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(54) **WIRELESS LOCAL AREA NETWORK (WLAN) USING UNIVERSAL FREQUENCY TRANSLATION TECHNOLOGY INCLUDING MULTI-PHASE EMBODIMENTS**

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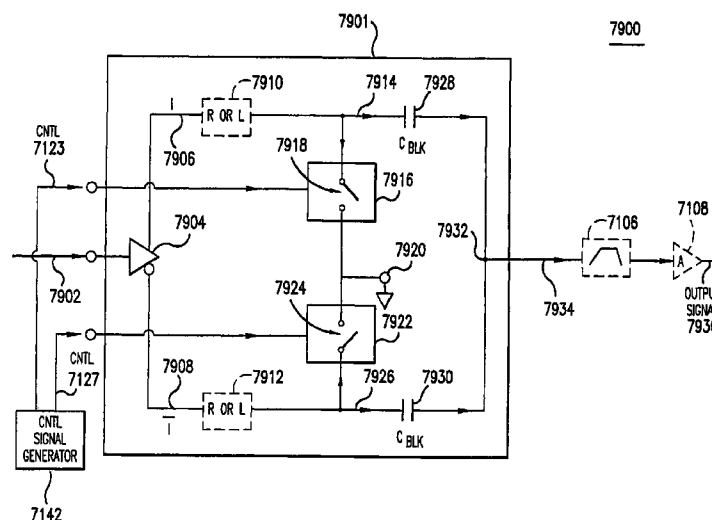
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(57) **ABSTRACT**

Frequency translation and applications of the same are described herein, including RF modem and wireless local area network (WLAN) applications. In embodiments, the WLAN invention includes an antenna, an LNA/PA module, a receiver, a transmitter, a control signal generator, a demodulation/modulation facilitation module, and a MAC interface. The WLAN receiver includes at least one universal frequency translation module that frequency down-converts a received EM signal. In embodiments, the UFT based receiver is configured in a multi-phase embodiment to reduce or eliminate re-radiation that is caused by DC offset. The WLAN transmitter includes at least one universal frequency translation module that frequency up-converts a baseband signal in preparation for transmission over the wireless LAN. In embodiments, the UFT based transmitter is configured in a differential and multi-phase embodiment to reduce carrier insertion and spectral growth.

**20 Claims, 349 Drawing Sheets**



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English-language Abstract of Japanese Patent Publication No. JP 7-169292, data supplied by ep.espacenet.com, 1 page (Jul. 4, 1995—Date of publication of application).

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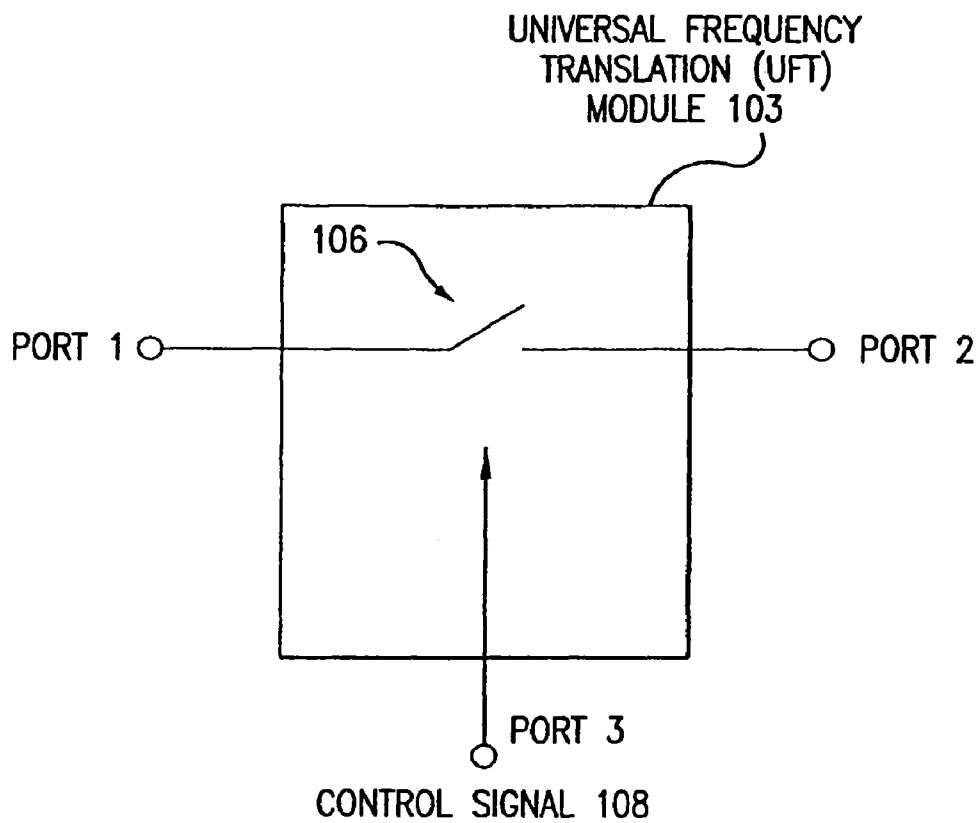
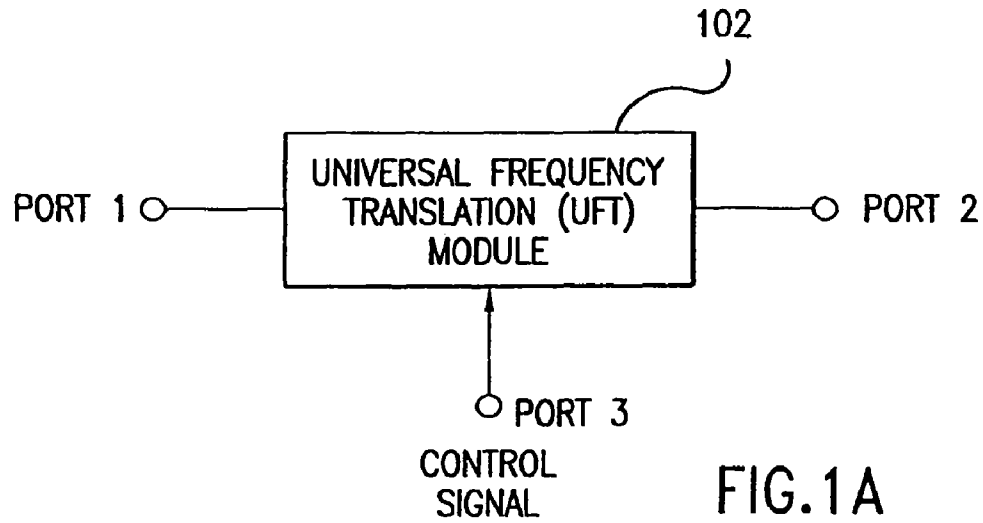
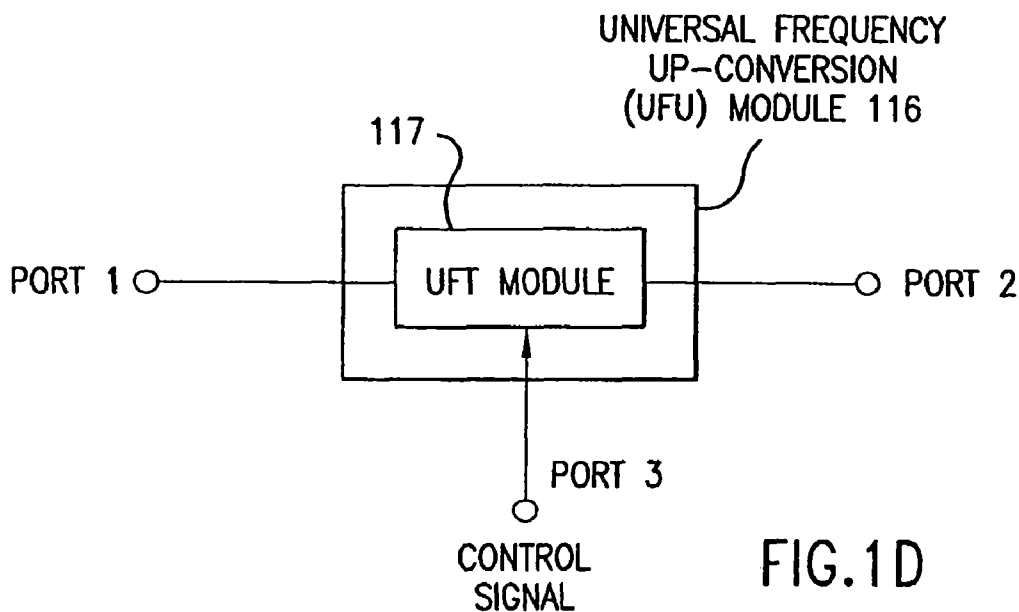
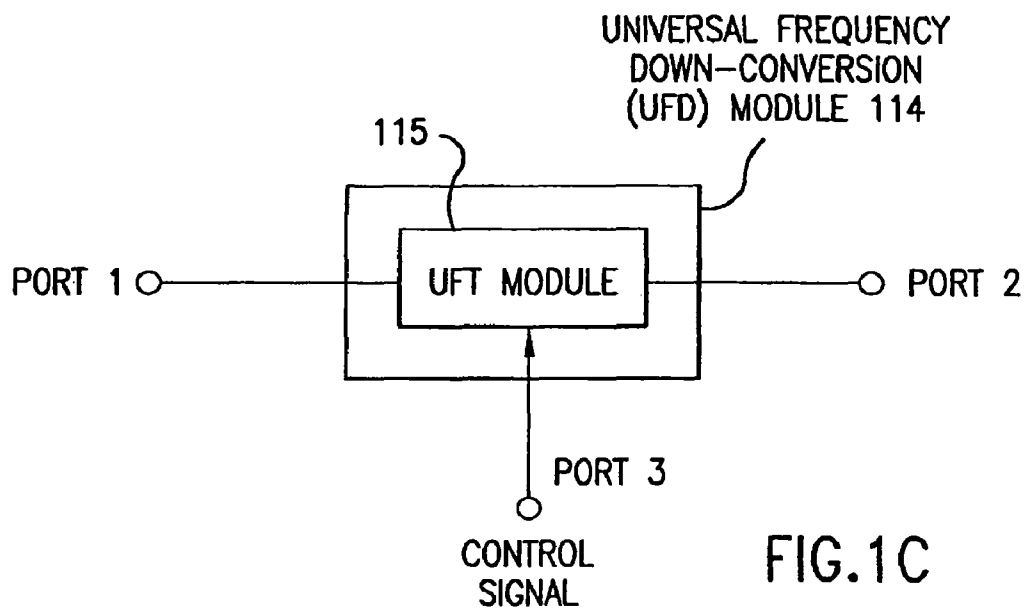
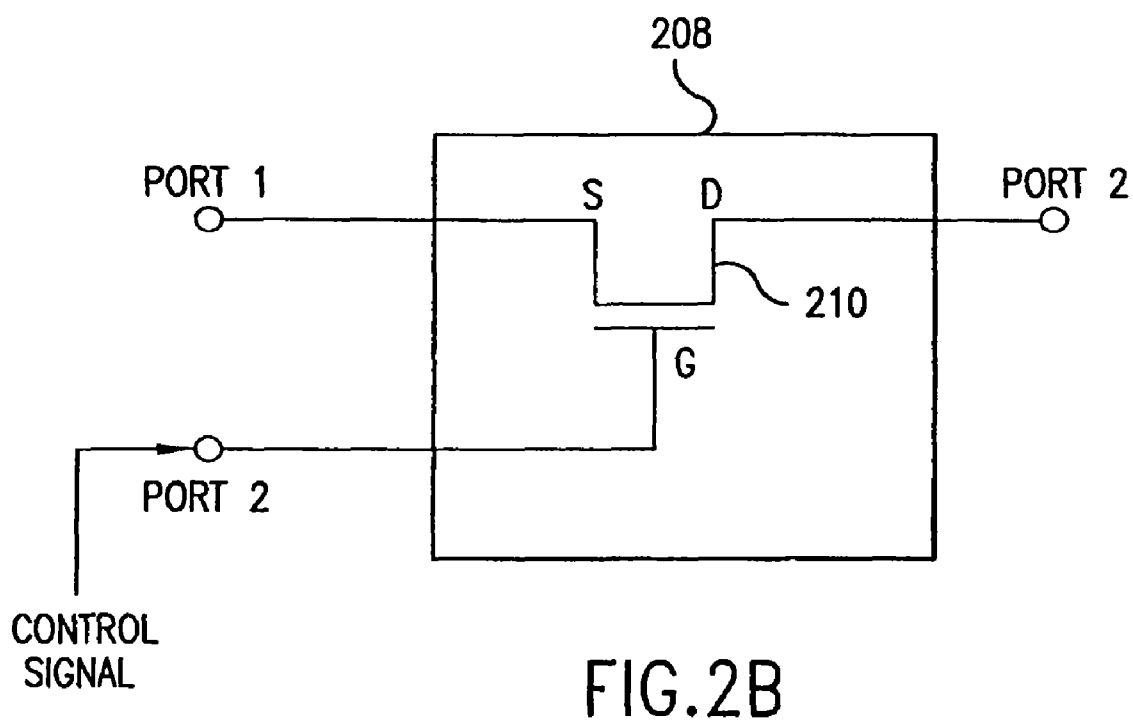
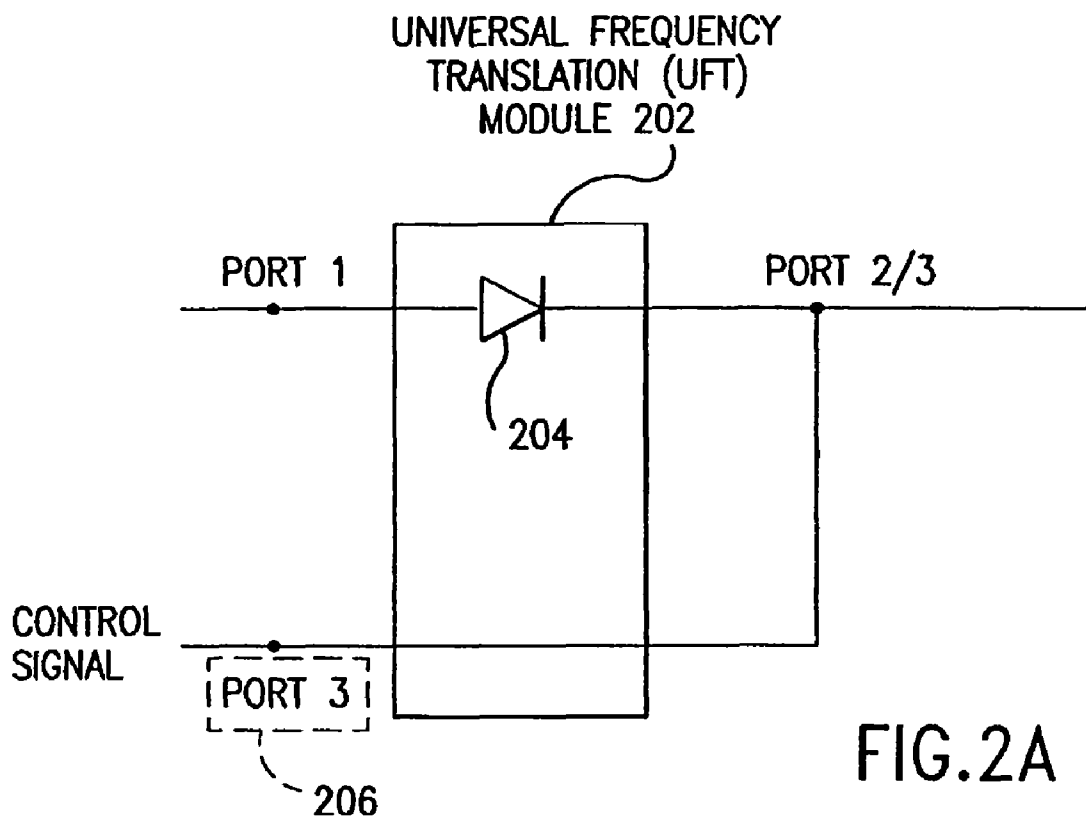
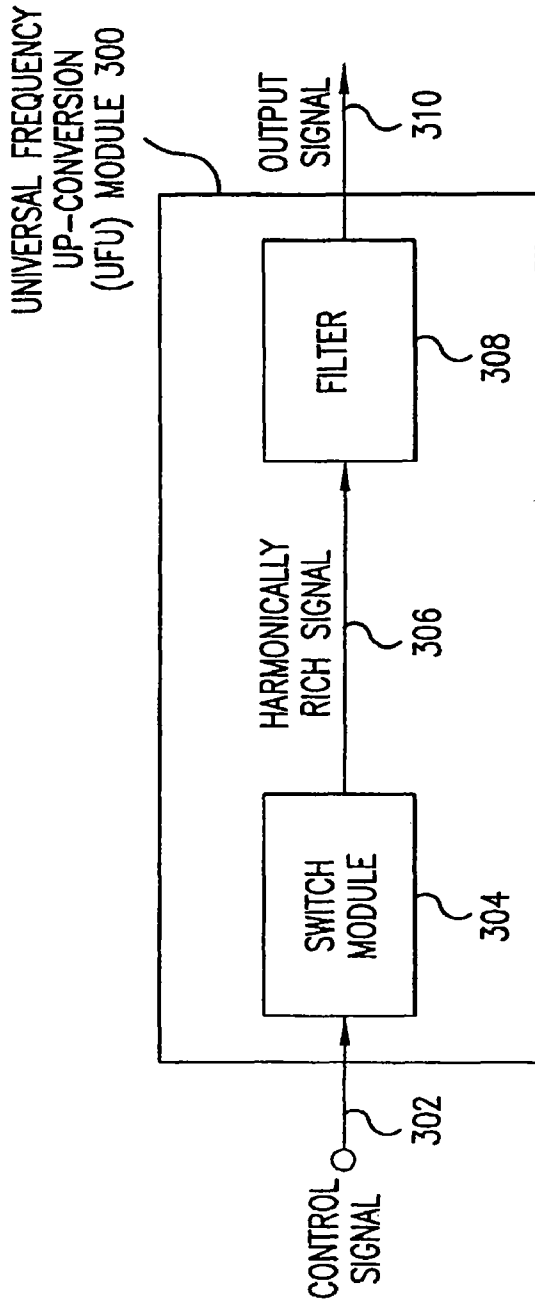


FIG. 1B







UNIVERSAL FREQUENCY  
UP-CONVERSION  
(UFU) MODULE 590

FIG.3

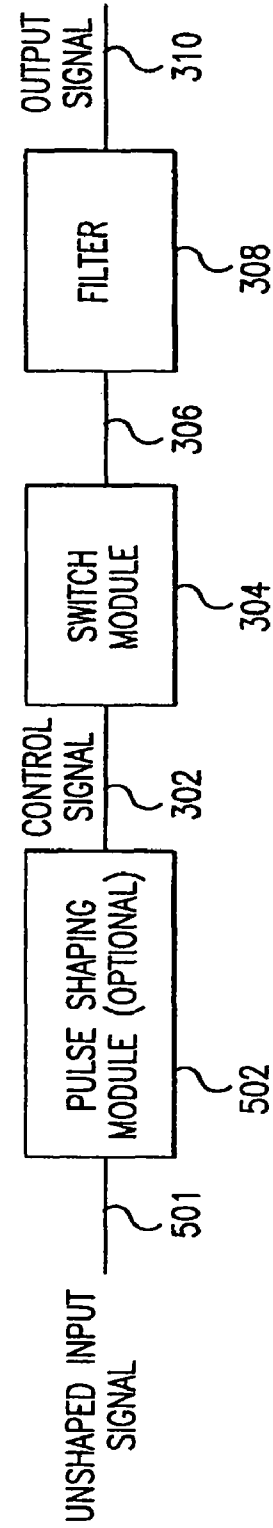


FIG.5

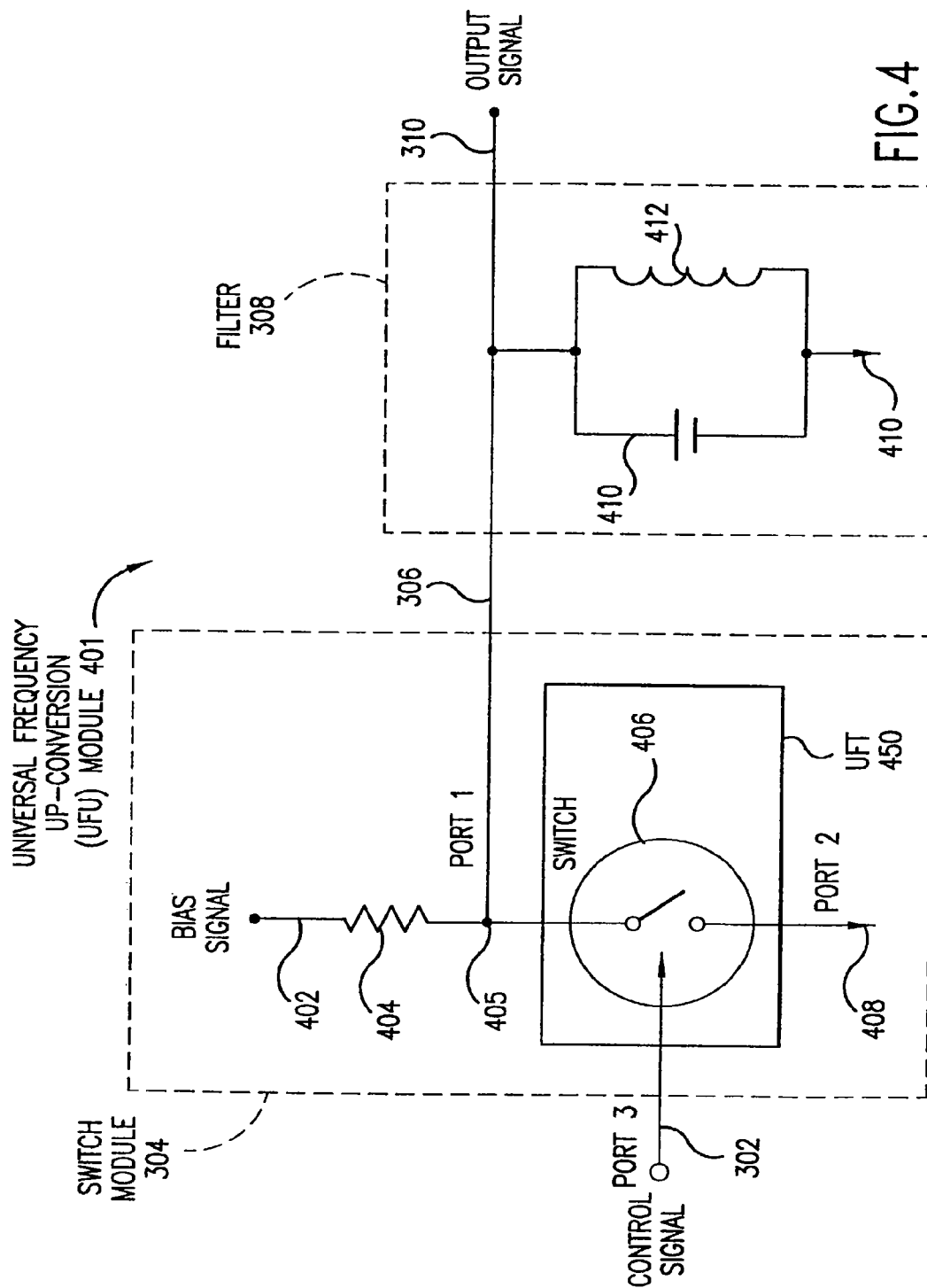
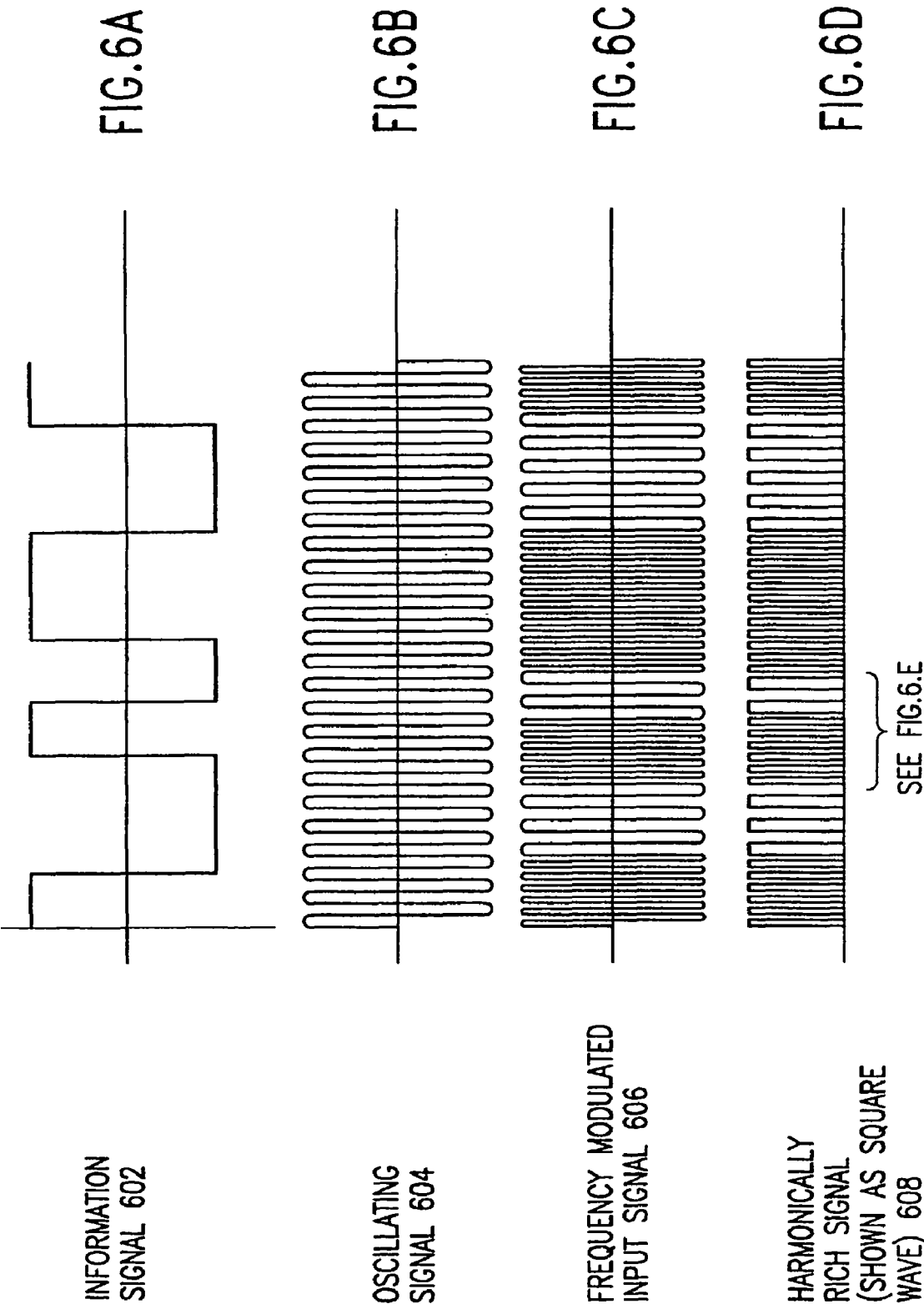
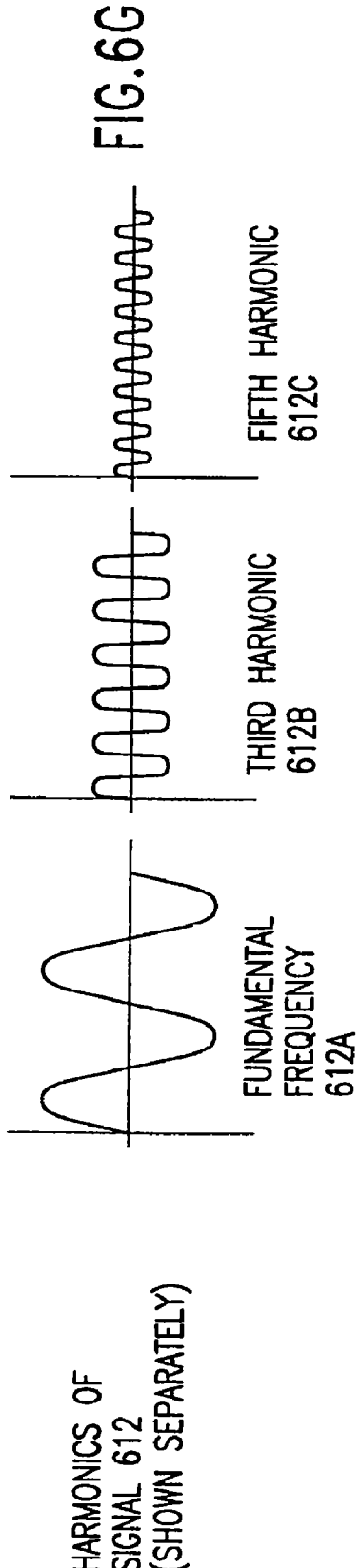
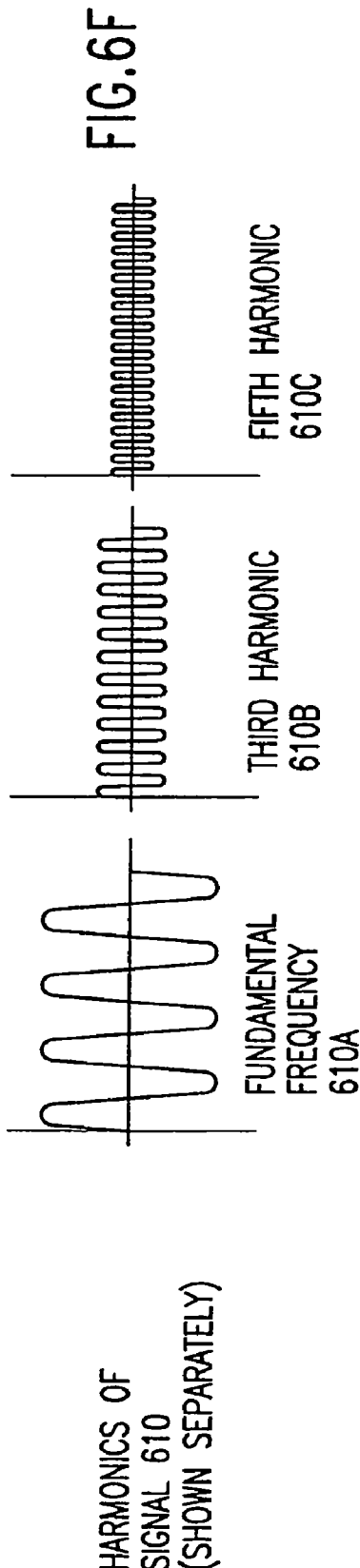
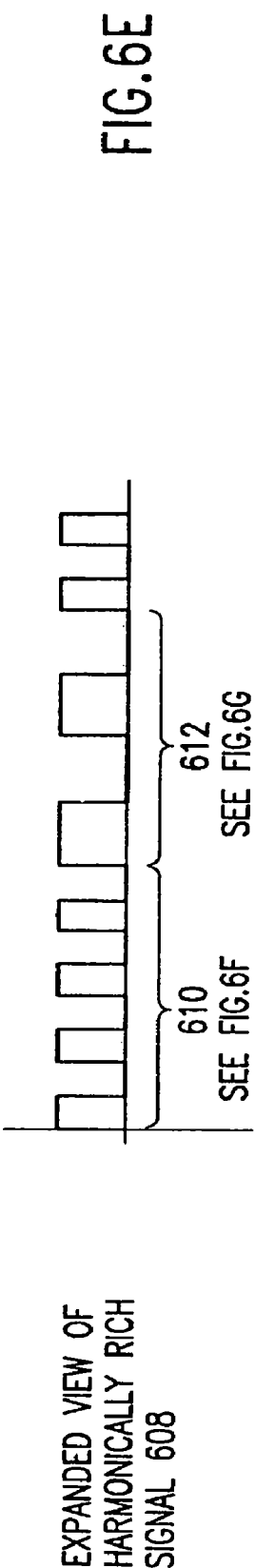
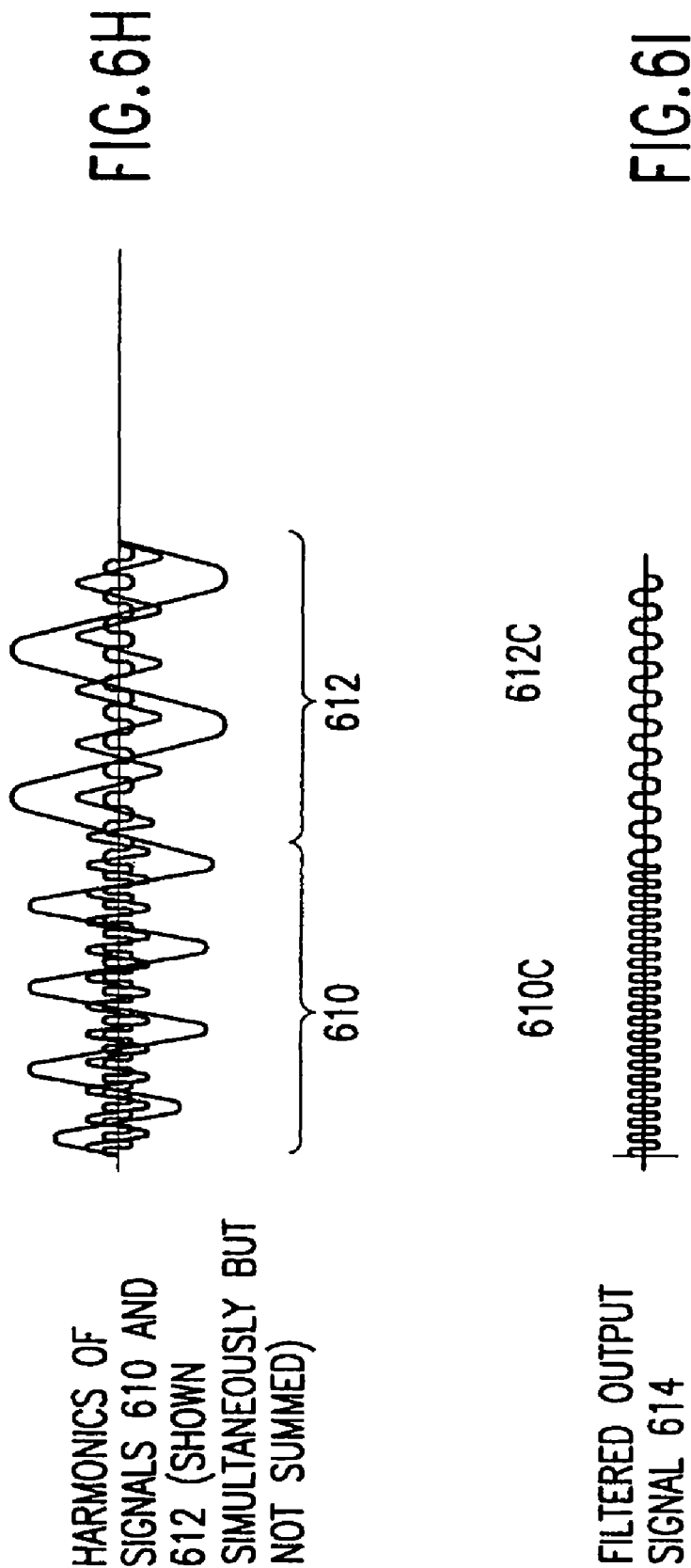


FIG. 4









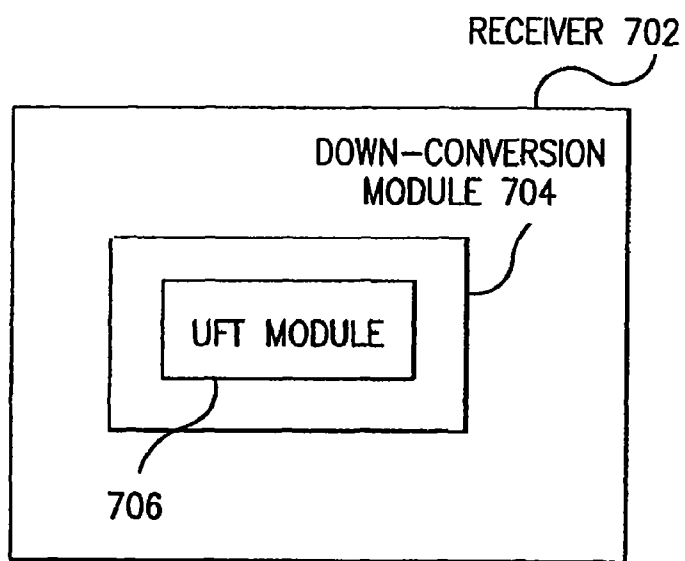


FIG. 7

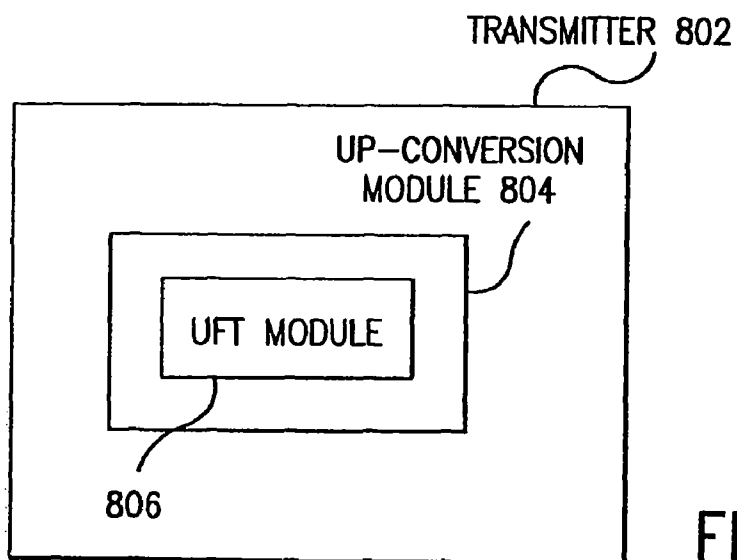


FIG. 8

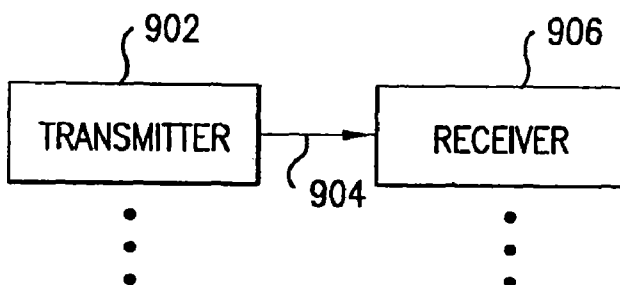


FIG. 9

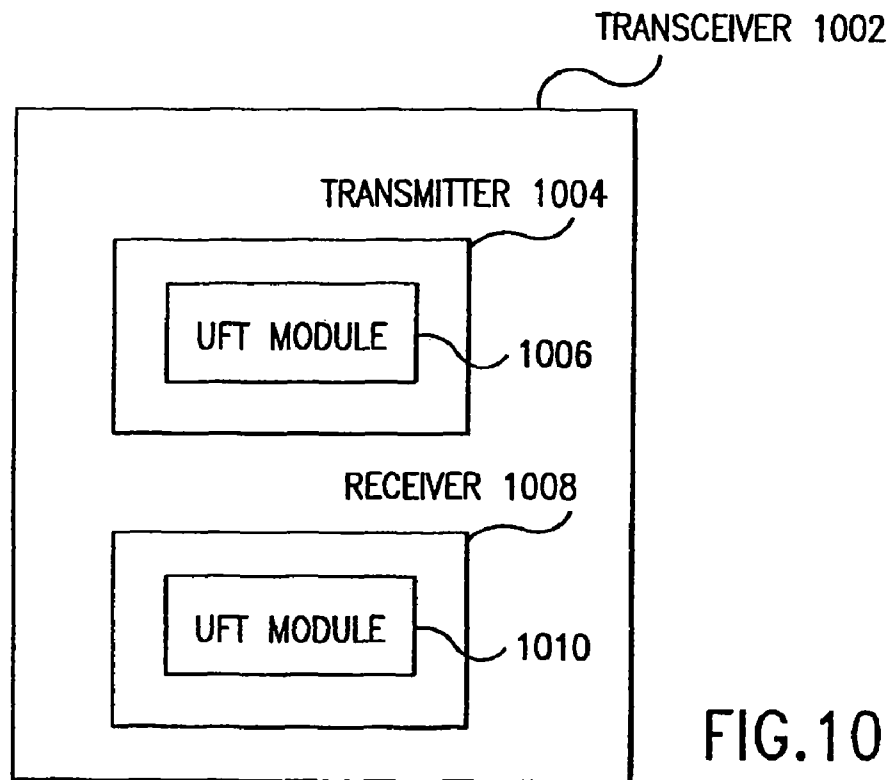


FIG. 10

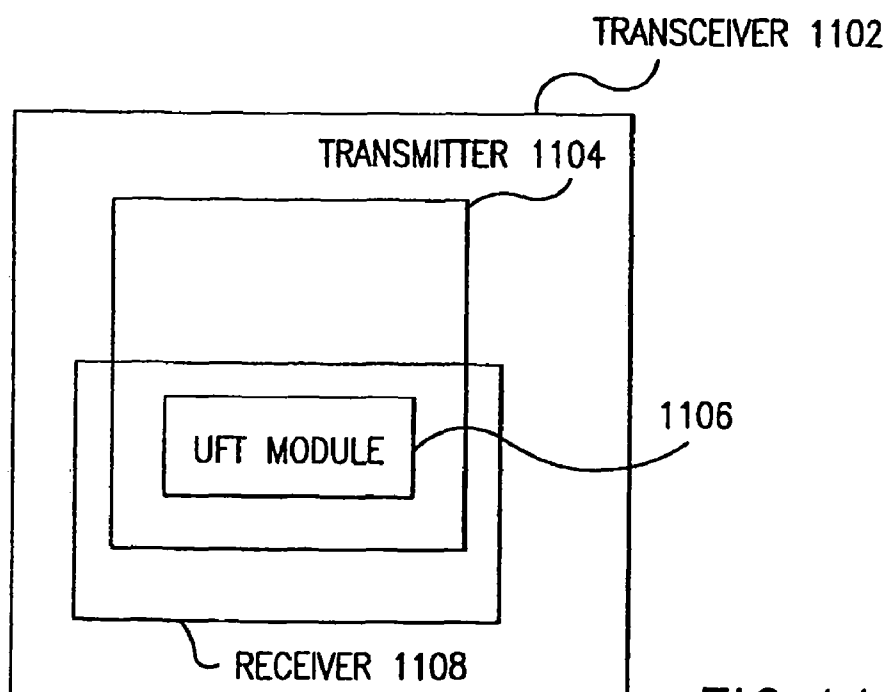


FIG. 11

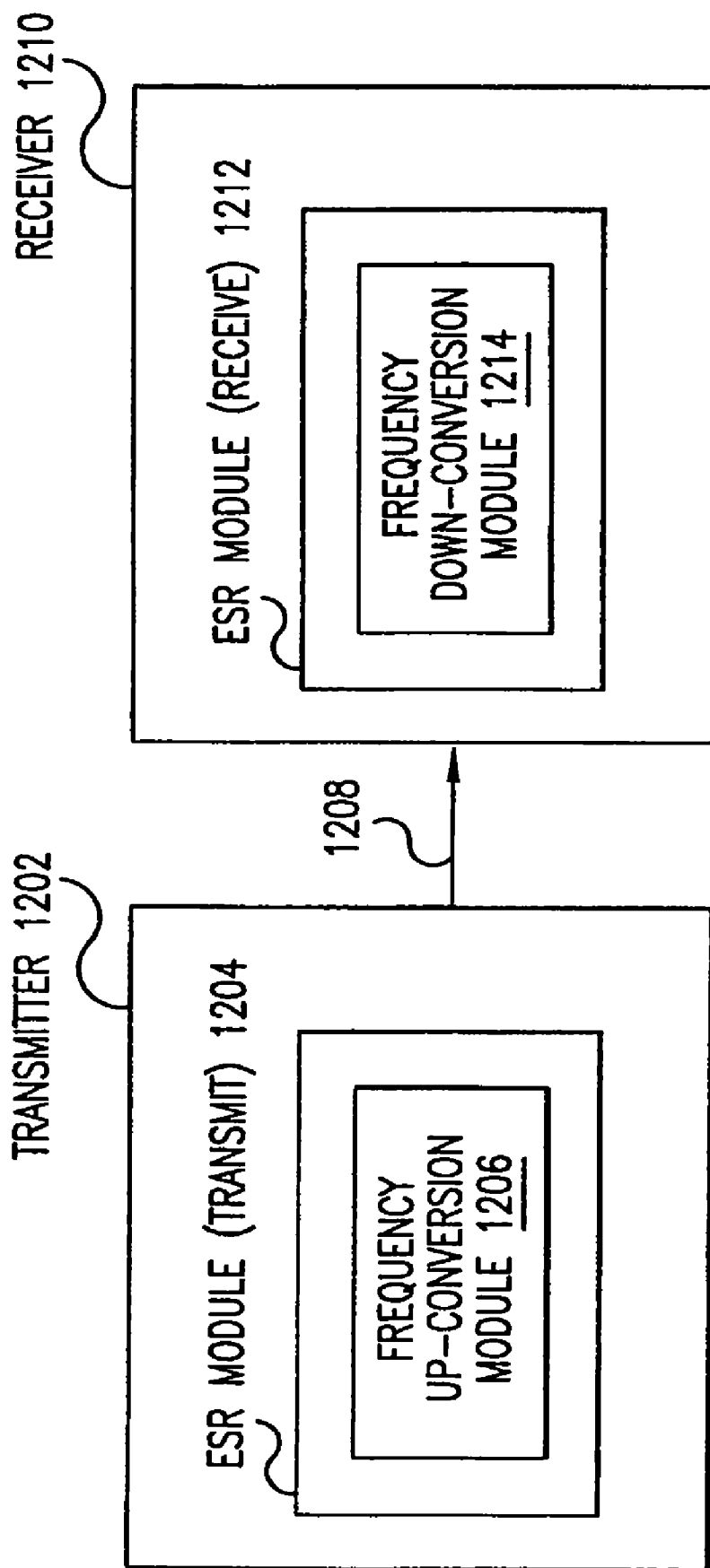


FIG.12

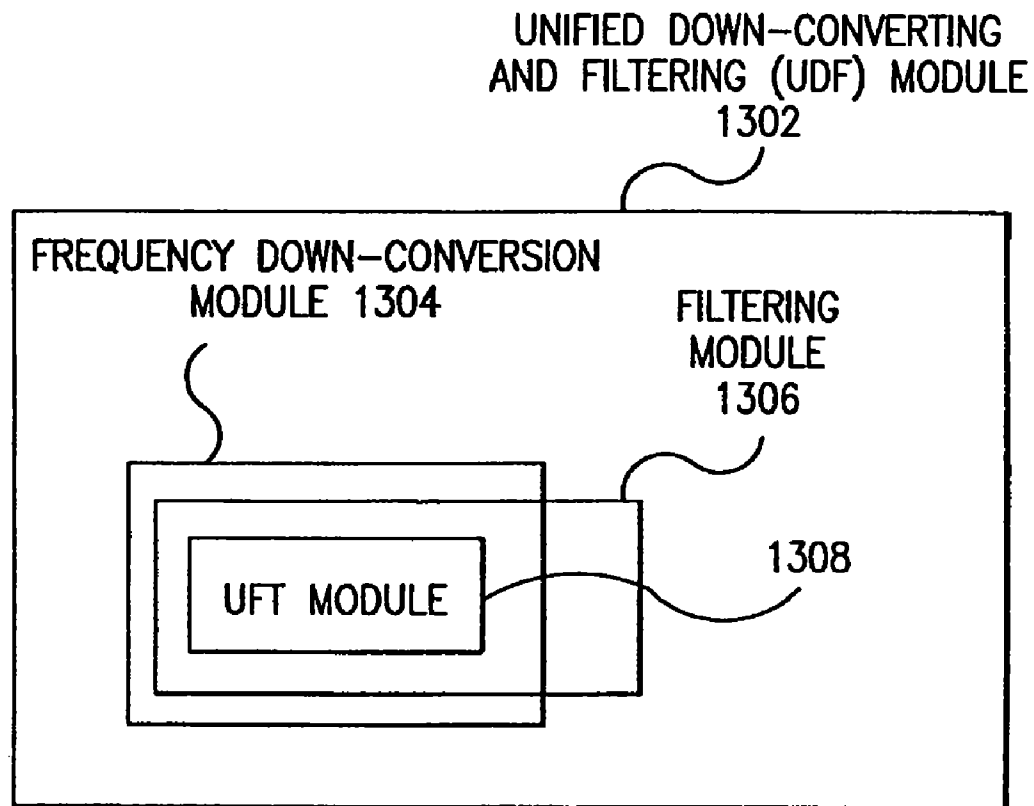


FIG.13

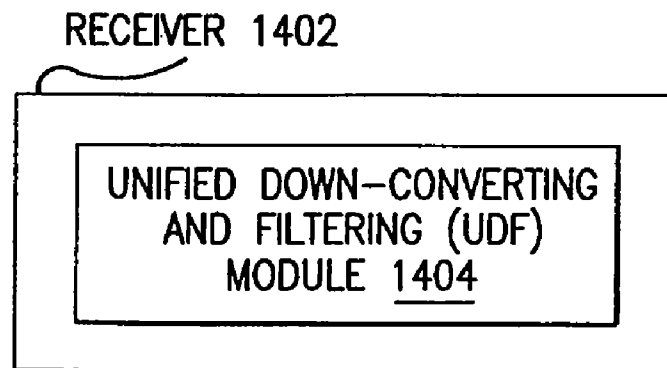


FIG.14

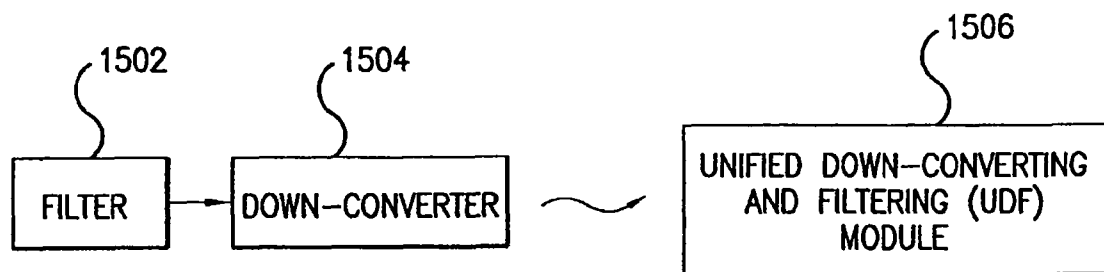


FIG. 15A

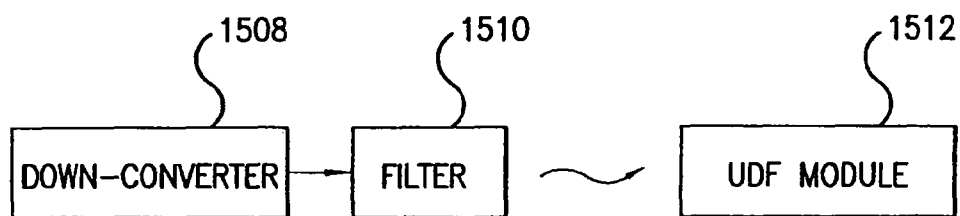


FIG. 15B

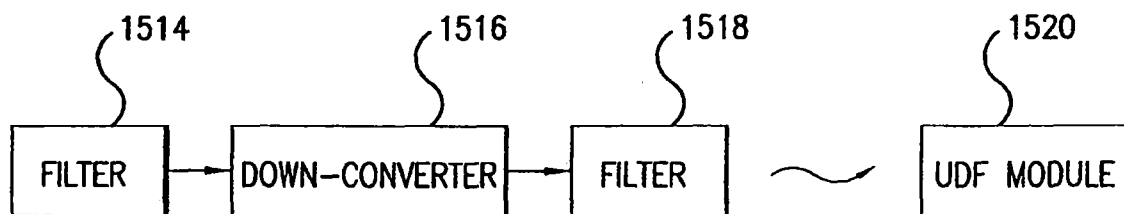


FIG. 15C





FIG. 15D

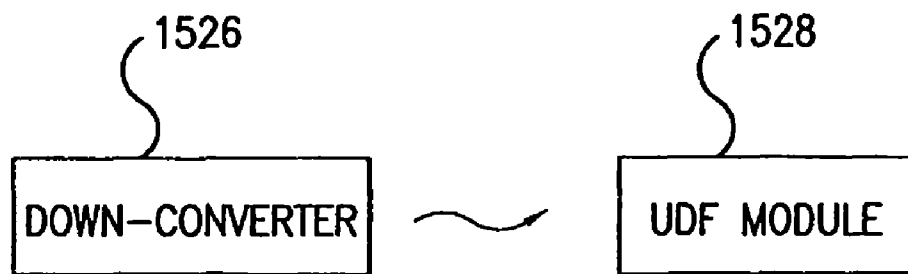


FIG. 15E



FIG. 15F

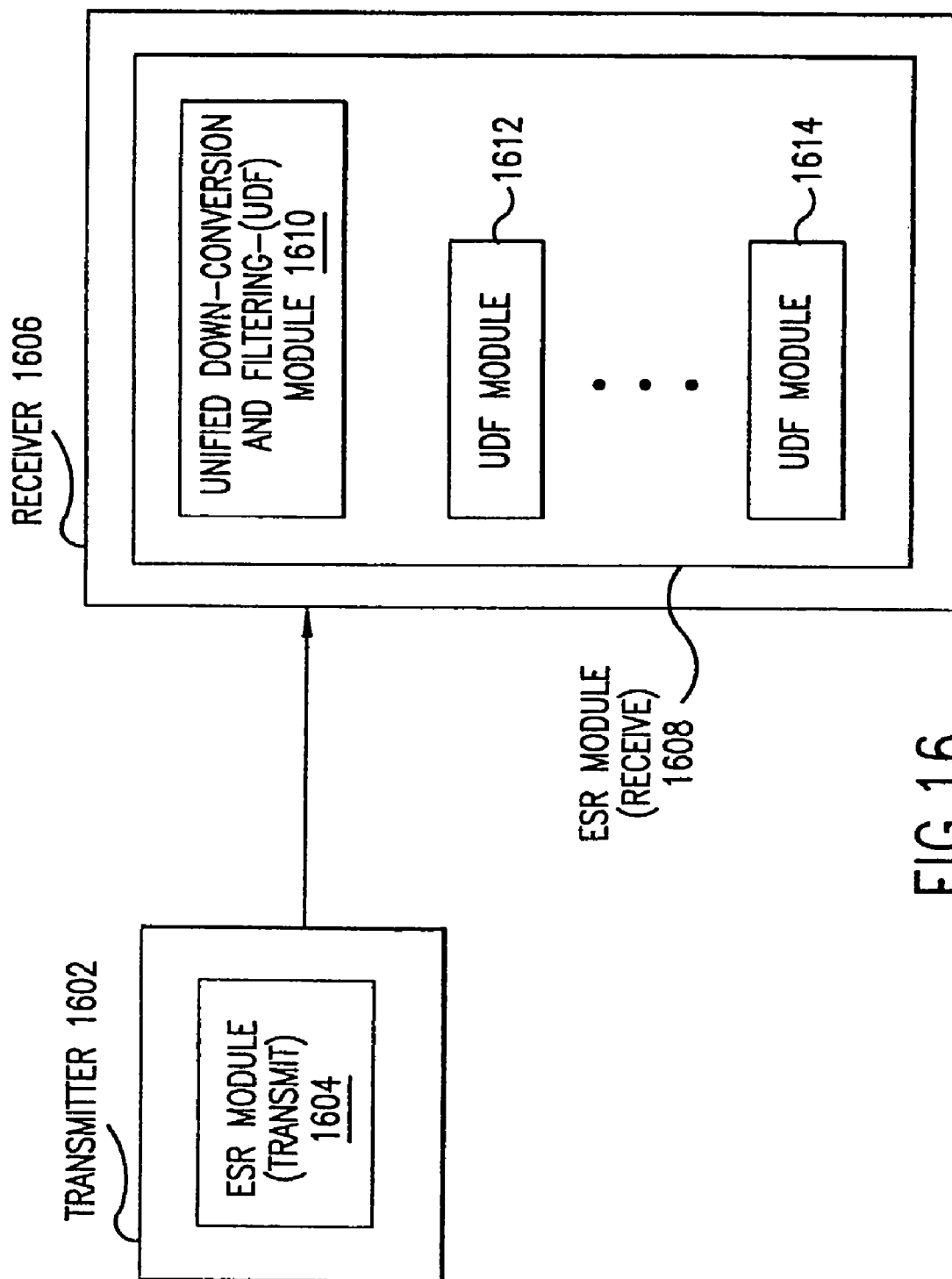


FIG.16

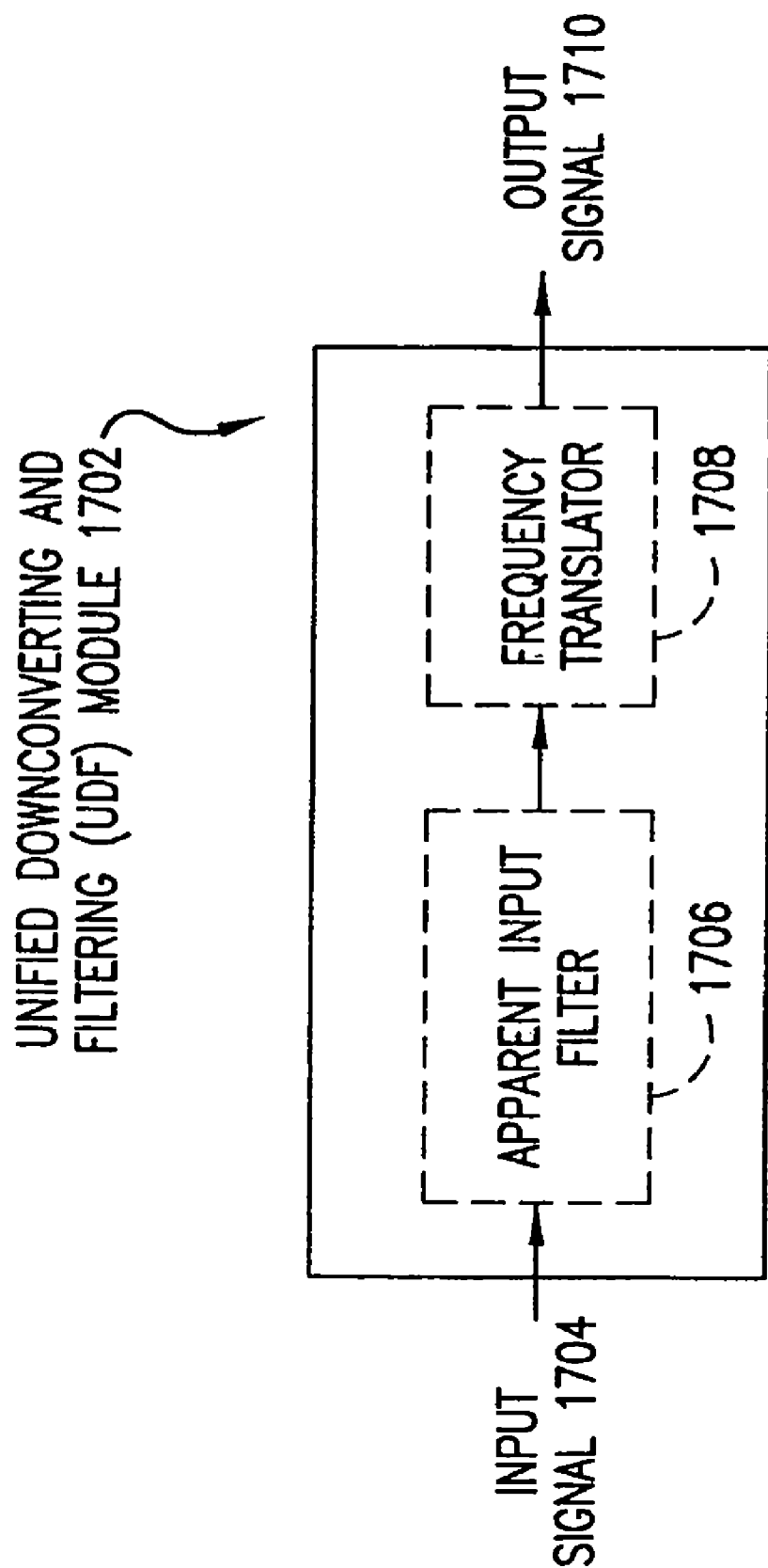


FIG.17

1802

TIME NODE	$t-1$ (RISING EDGE OF $\phi_1$ )	$t-1$ (RISING EDGE OF $\phi_2$ )	$t$ (RISING EDGE OF $\phi_1$ )	$t$ (RISING EDGE OF $\phi_2$ )	$t+1$ (RISING EDGE OF $\phi_1$ )
1902	$V_{I\ t-1}$ 1804	$V_{I\ t-1}$ 1808	$V_{I\ t}$ 1816	$V_{I\ t}$ 1826	$V_{I\ t+1}$ 1838
1904	—	$V_{I\ t-1}$ 1810	$V_{I\ t-1}$ 1818	$V_{I\ t}$ 1828	$V_{I\ t}$ 1840
1906	$V_{O\ t-1}$ 1806	$V_{O\ t-1}$ 1812	$V_{O\ t}$ 1820	$V_{O\ t}$ 1830	$V_{O\ t+1}$ 1842
1908	—	$V_{O\ t-1}$ 1814	$V_{O\ t-1}$ 1822	$V_{O\ t}$ 1832	$V_{O\ t}$ 1844
1910	— 1807	—	$V_{O\ t-1}$ 1824	$V_{O\ t-1}$ 1834	$V_{O\ t}$ 1846
1912	—	— 1815	—	$V_{O\ t-1}$ 1836	$V_{O\ t-1}$ 1848
1918	—	—	—	—	$V_{I\ t}^-$ 1850 $0.1 * V_{O\ t}$ $0.8 * V_{O\ t-1}$

FIG.18

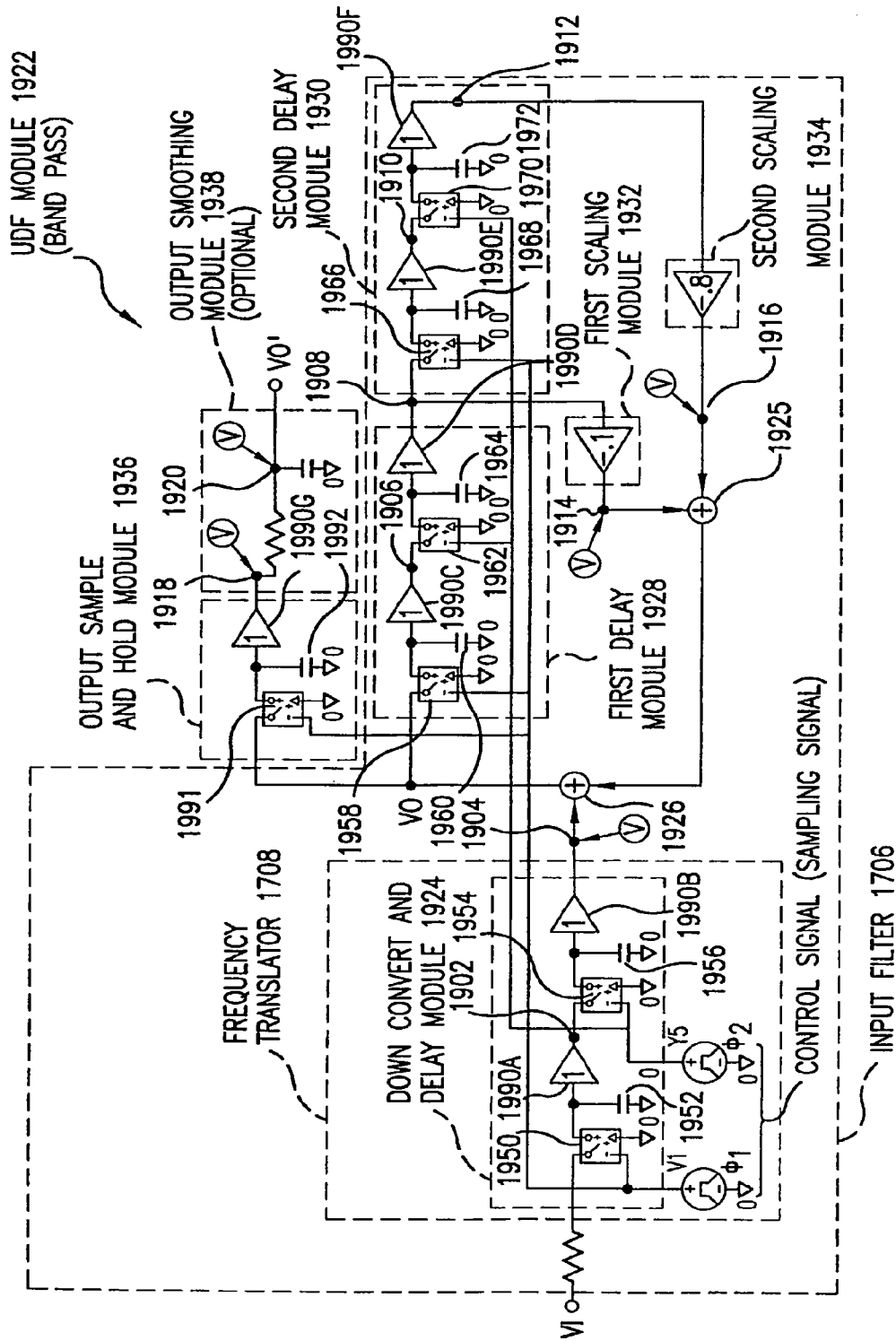


FIG. 19

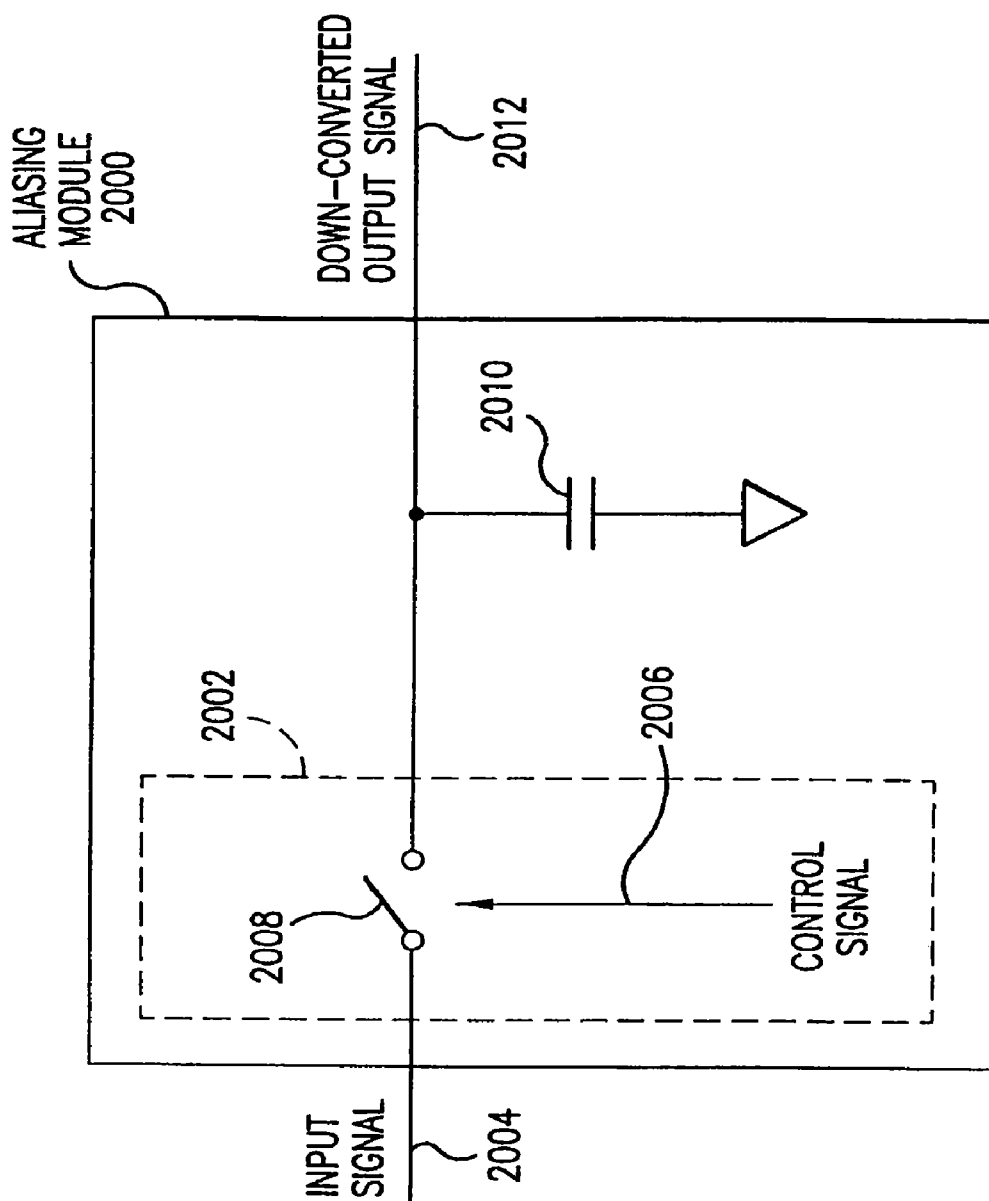


FIG. 20A

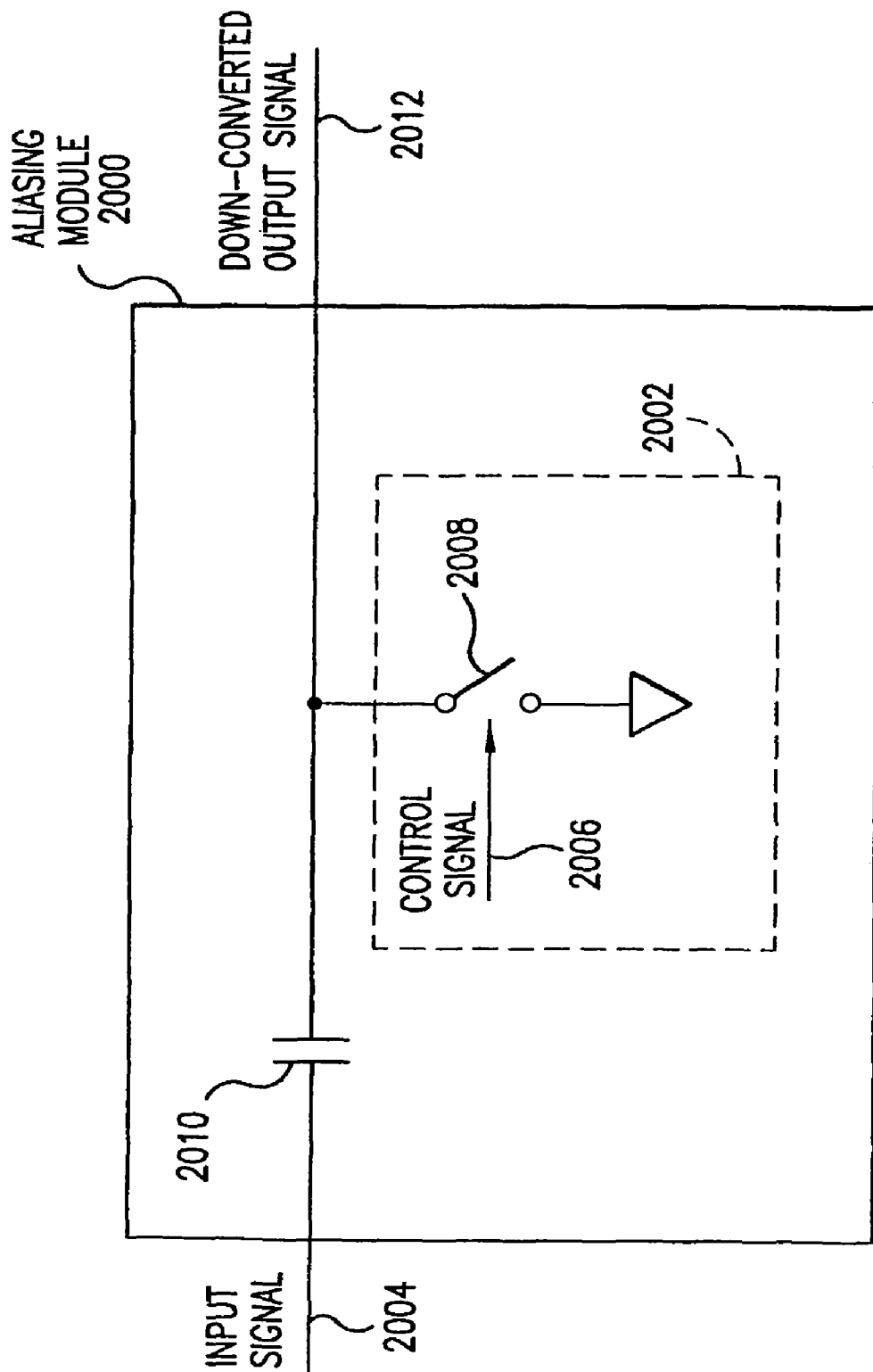


FIG. 20A-1

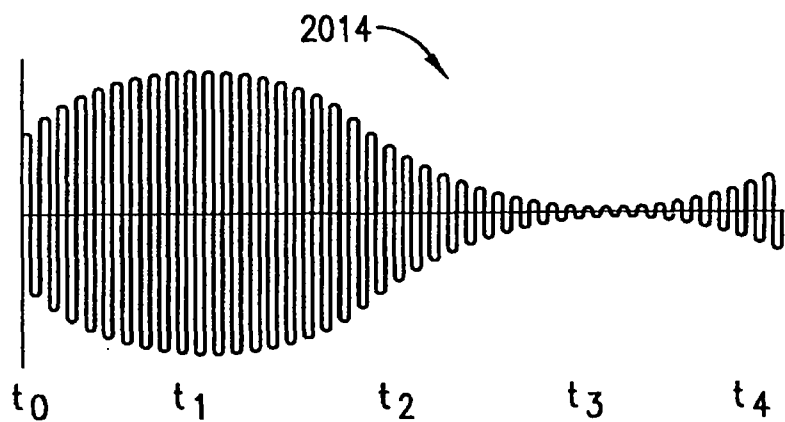


FIG. 20B

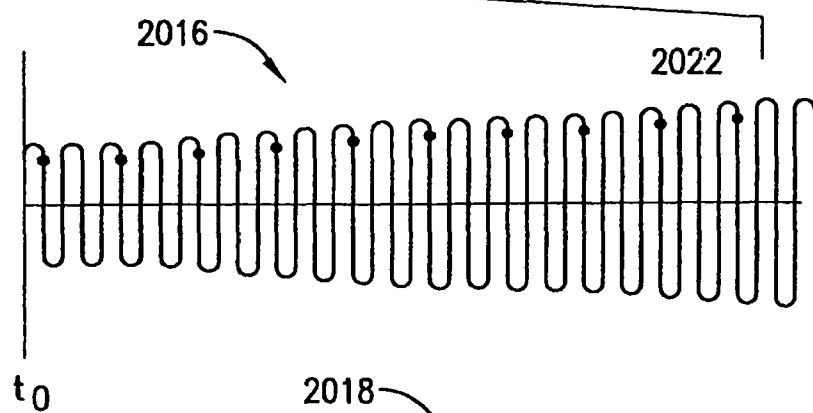


FIG. 20C

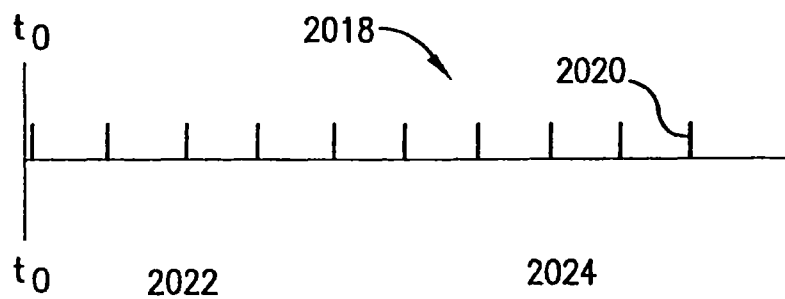


FIG. 20D

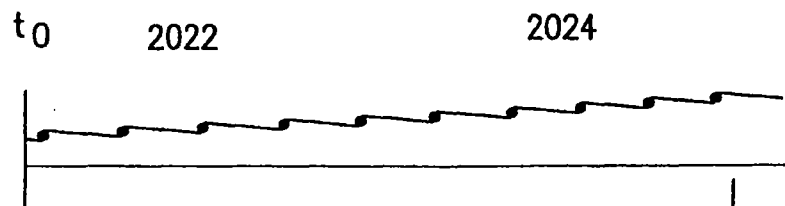


FIG. 20E

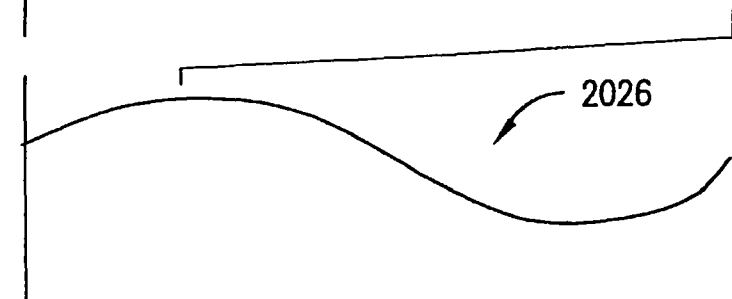
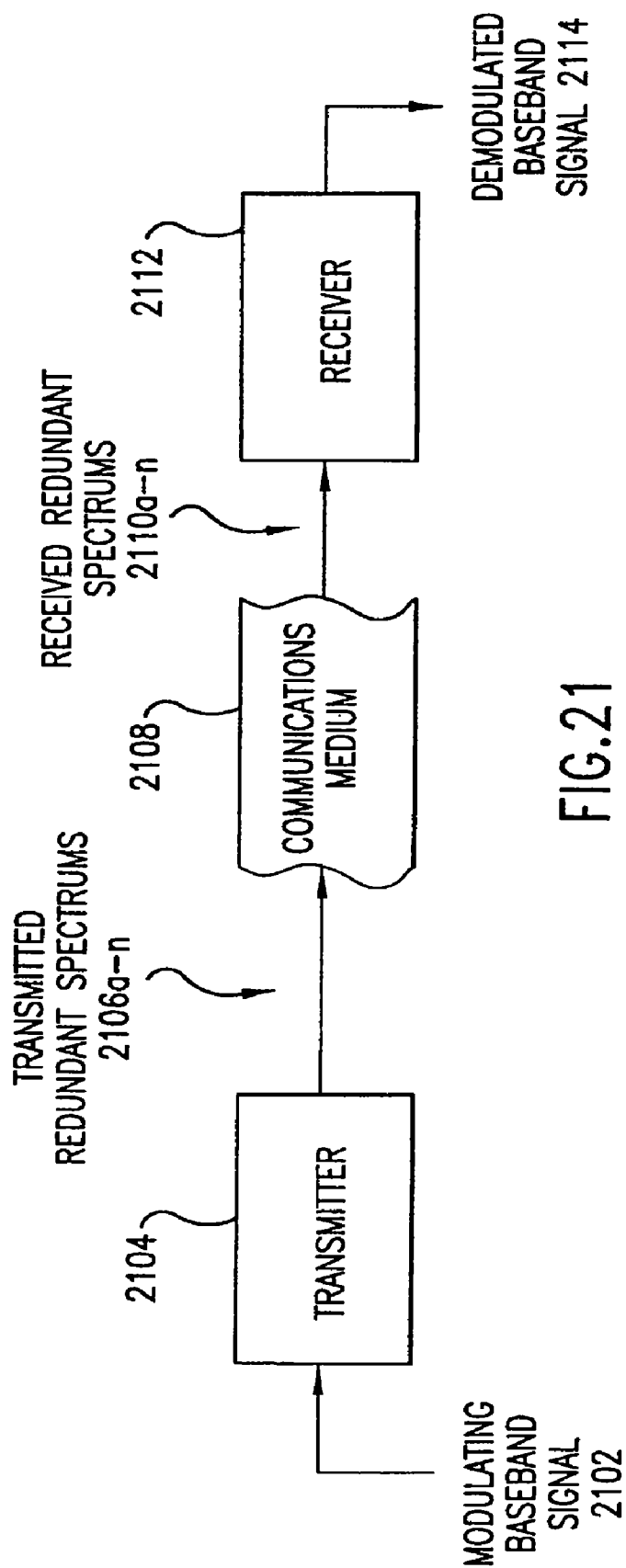


FIG. 20F





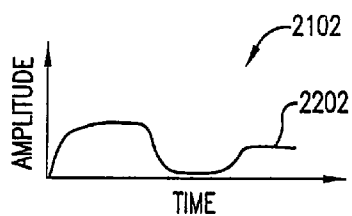


FIG. 22A

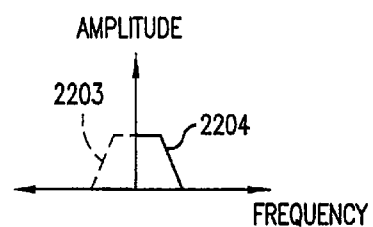


FIG. 22B

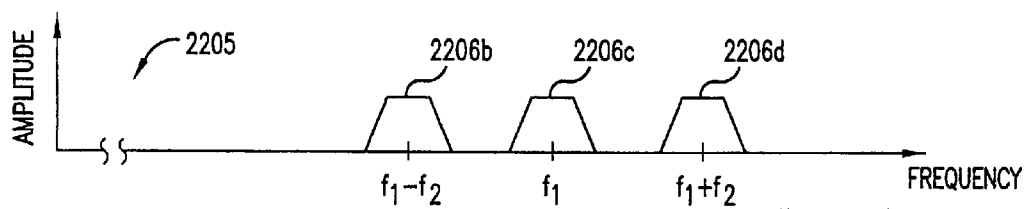


FIG. 22C

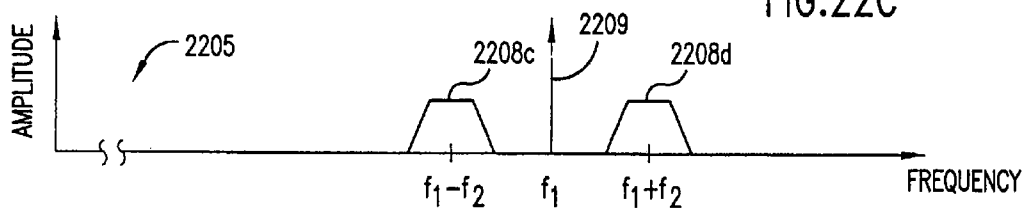


FIG. 22D

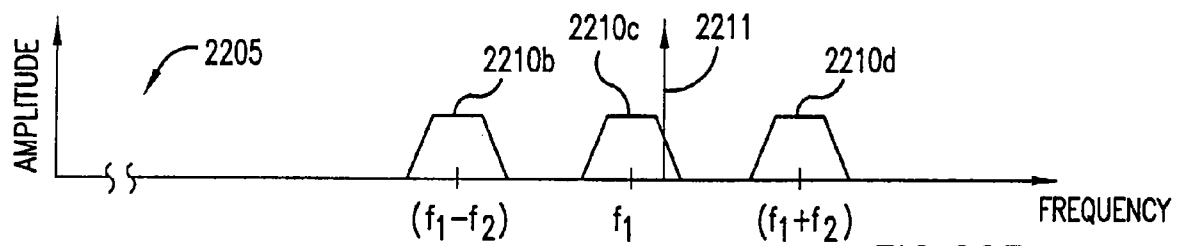


FIG. 22E

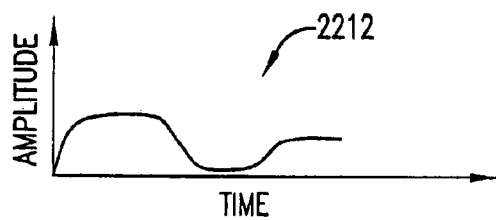


FIG. 22F

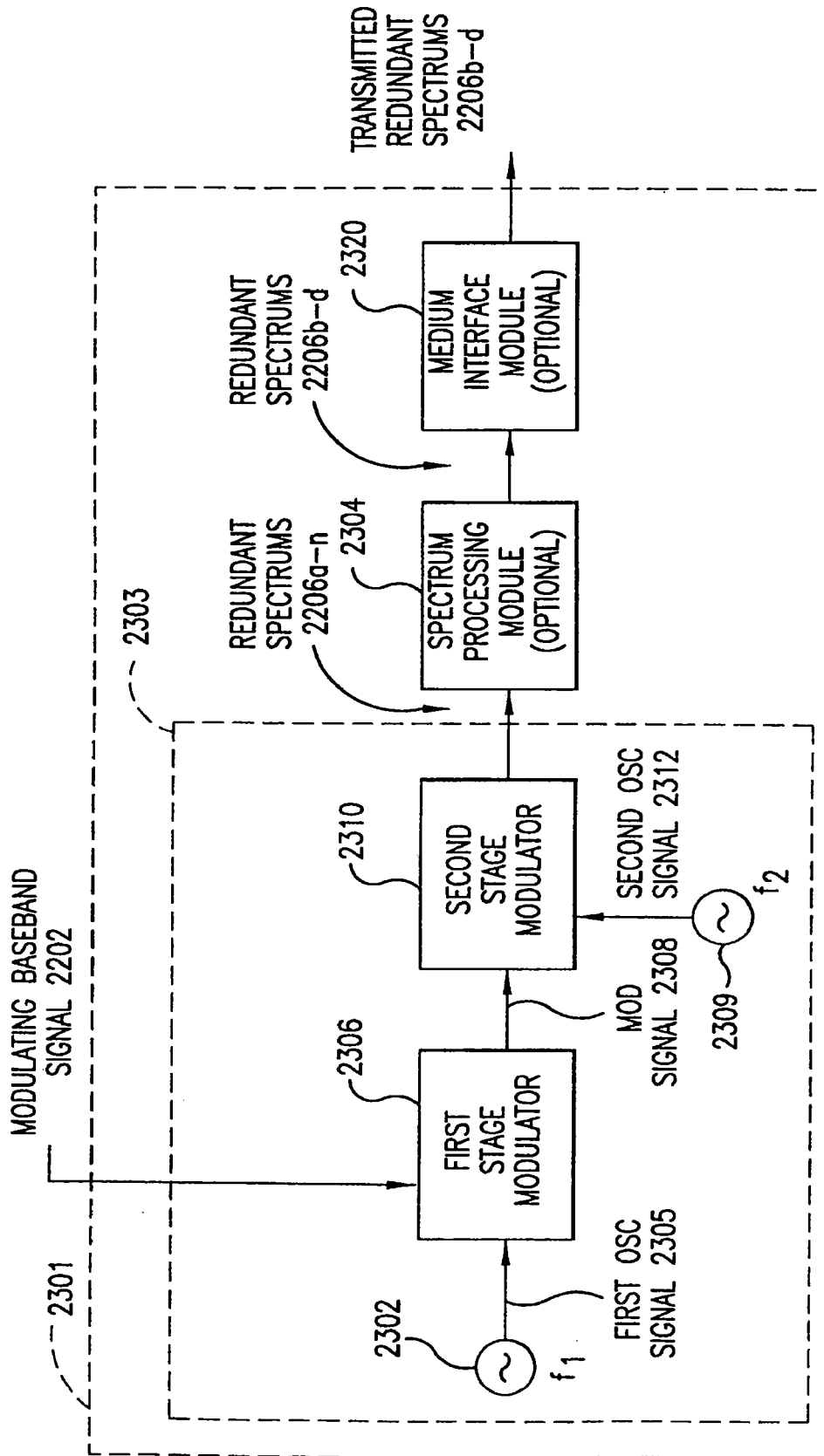


FIG. 23A

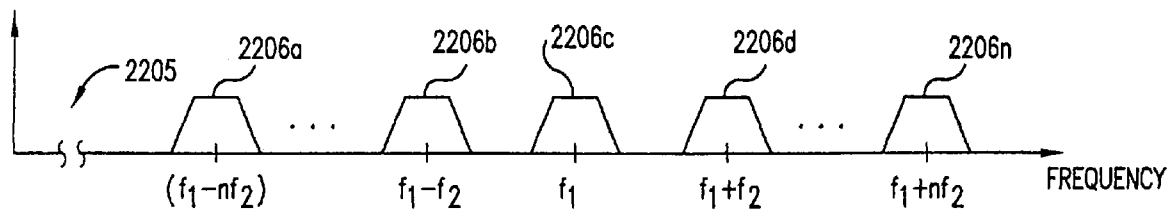


FIG. 23B

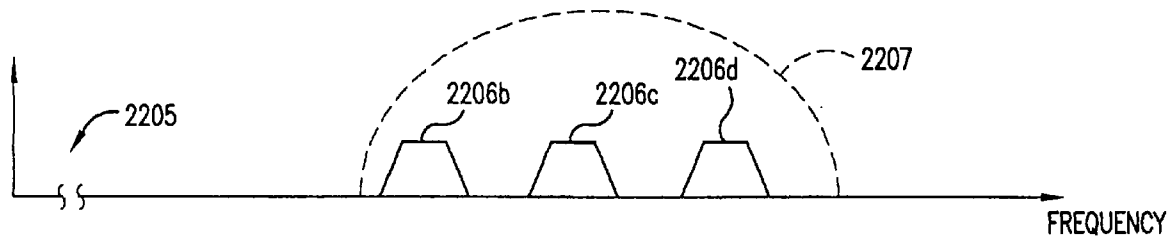


FIG. 23C

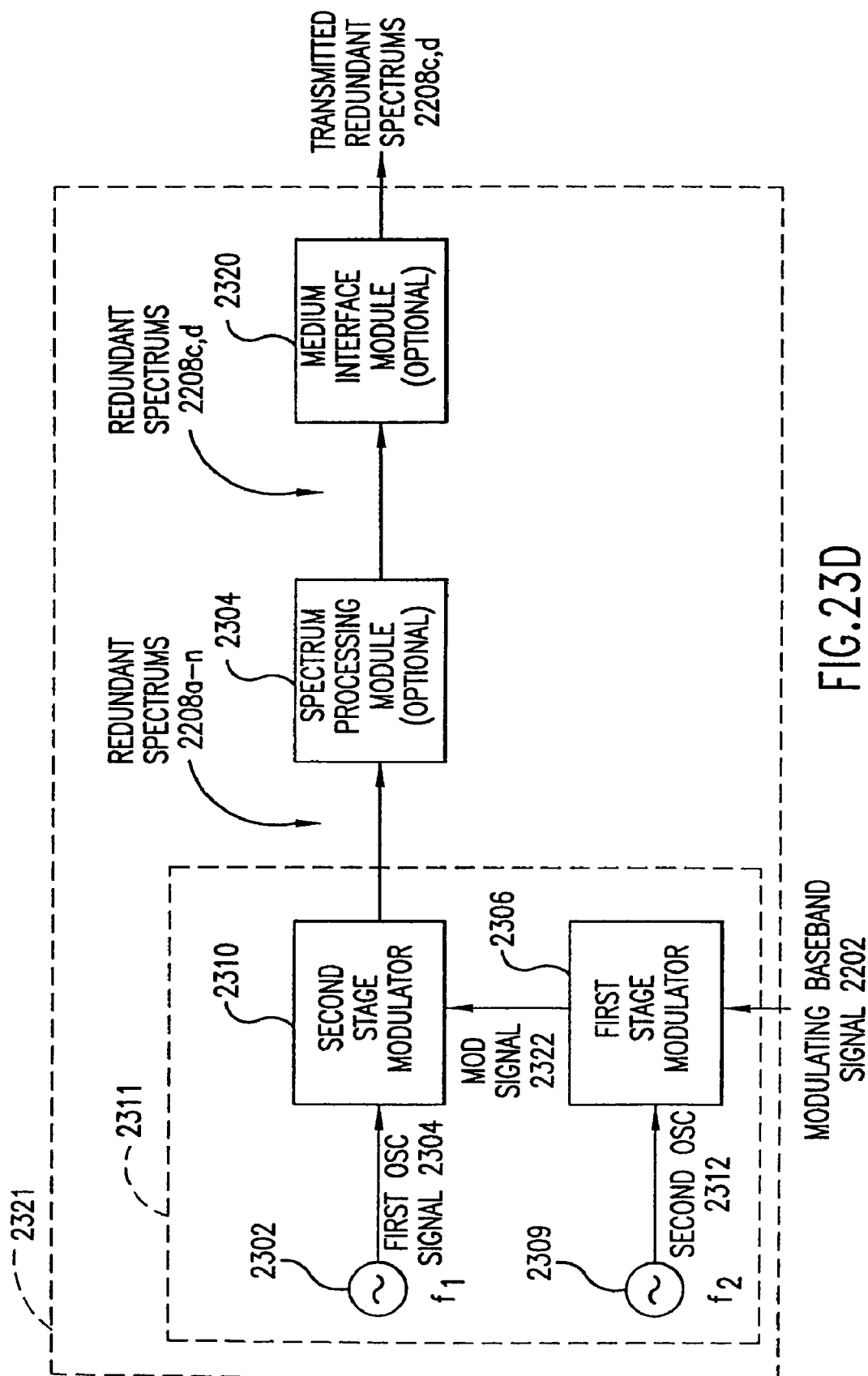


FIG. 23D

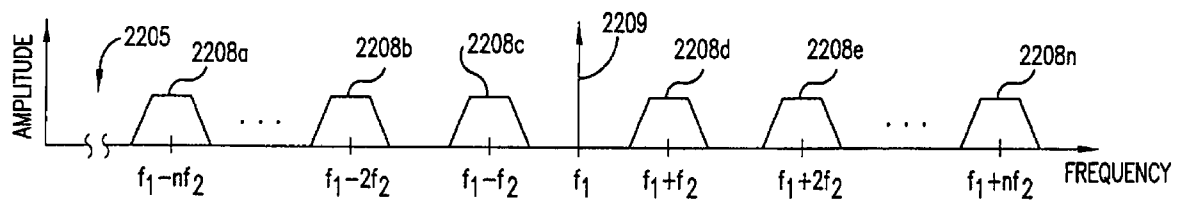


FIG. 23E

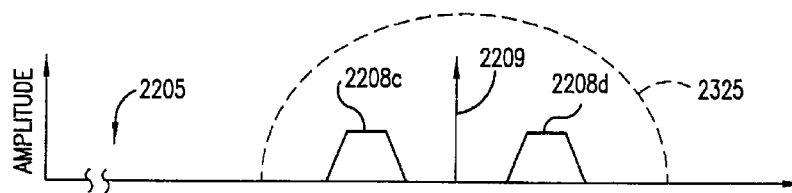
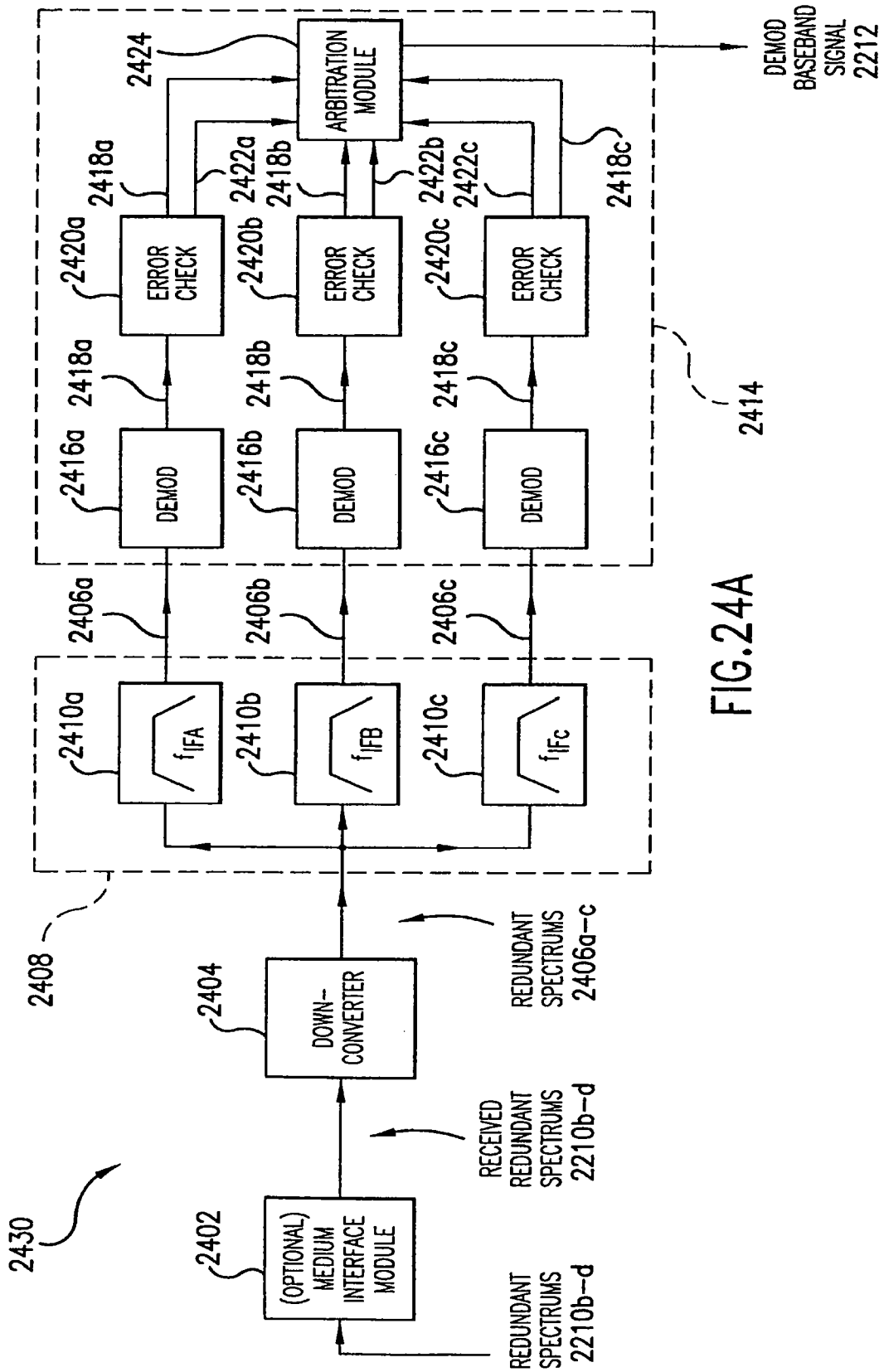


FIG. 23F





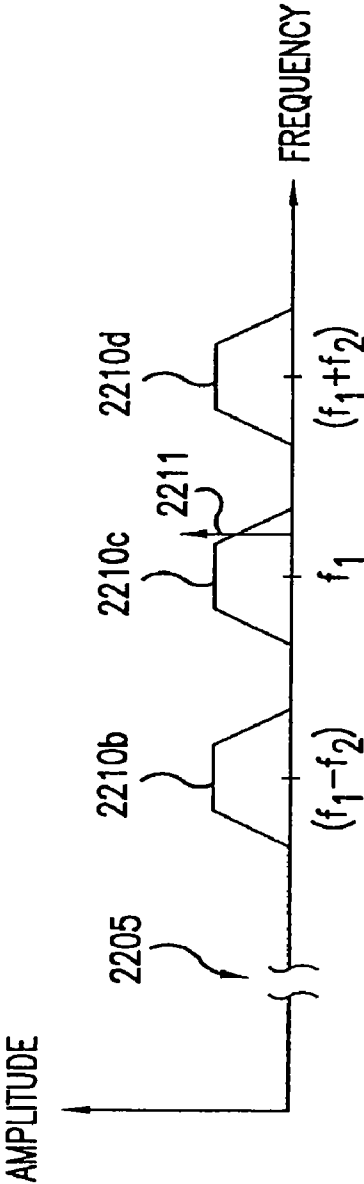


FIG. 24B

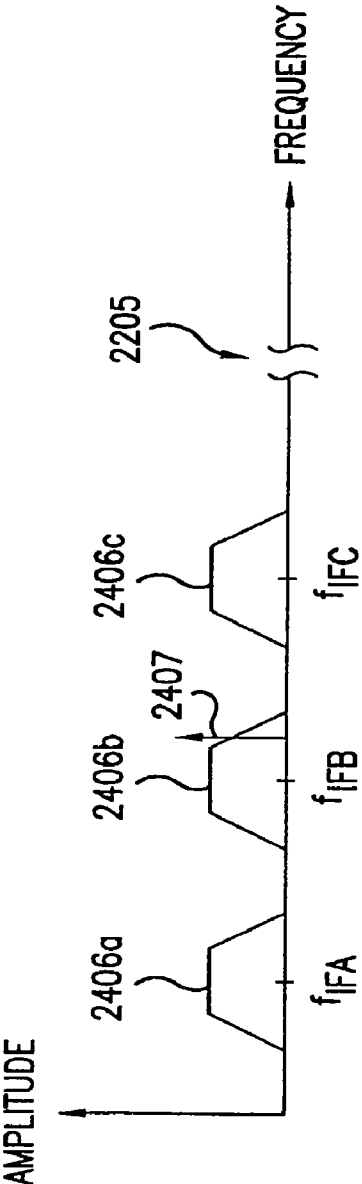
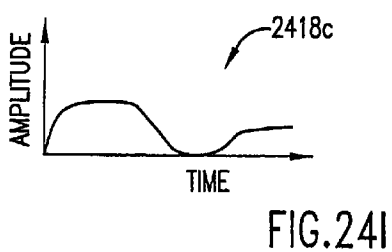
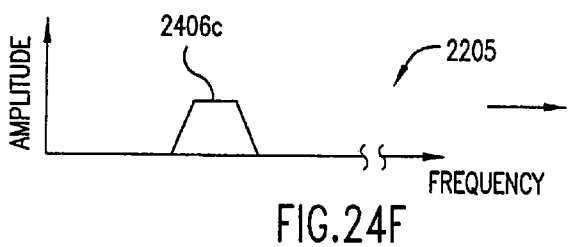
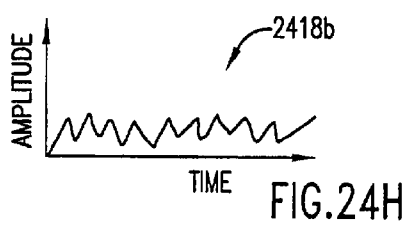
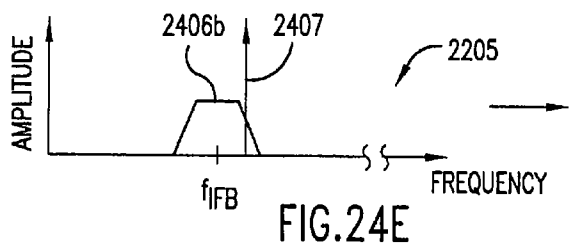
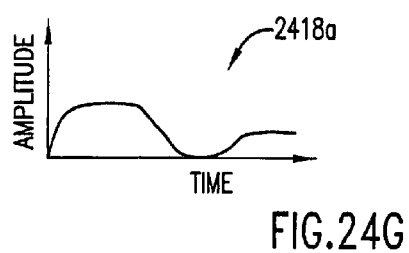
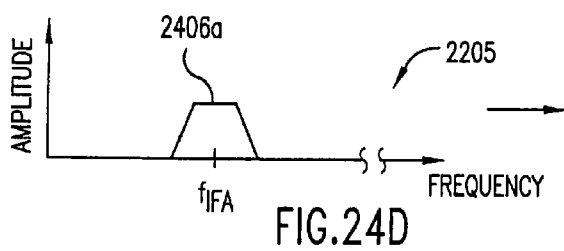


FIG. 24C



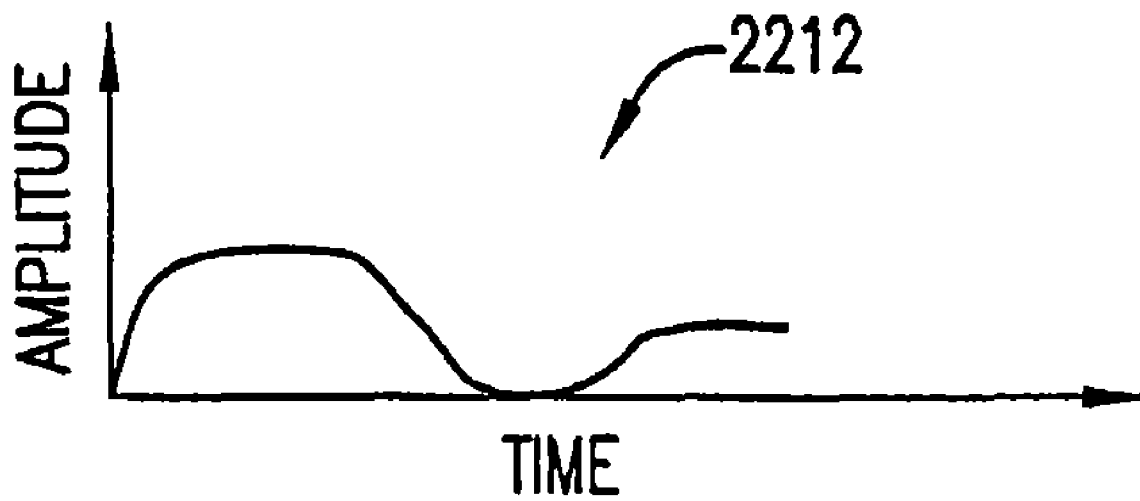


FIG.24J

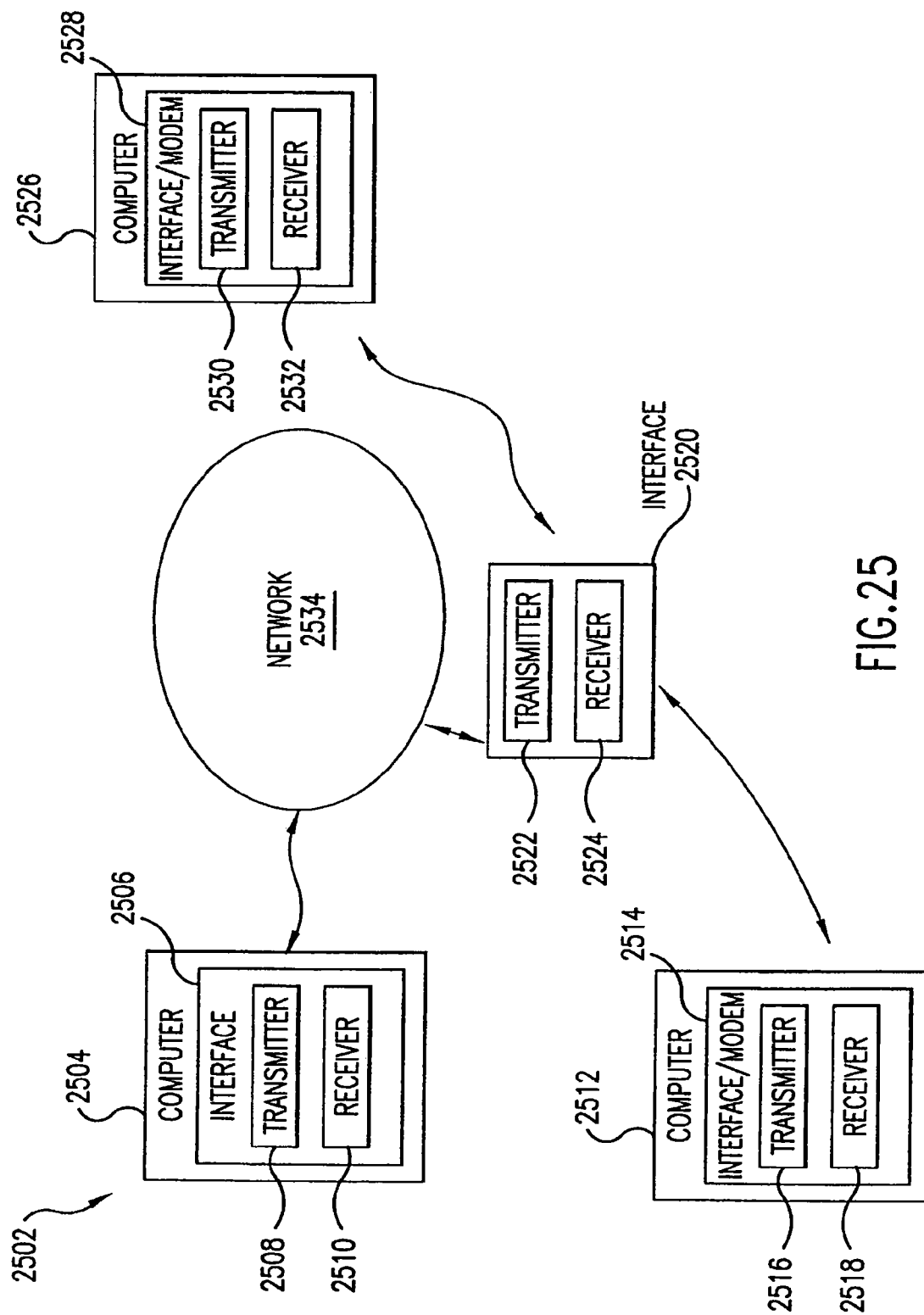
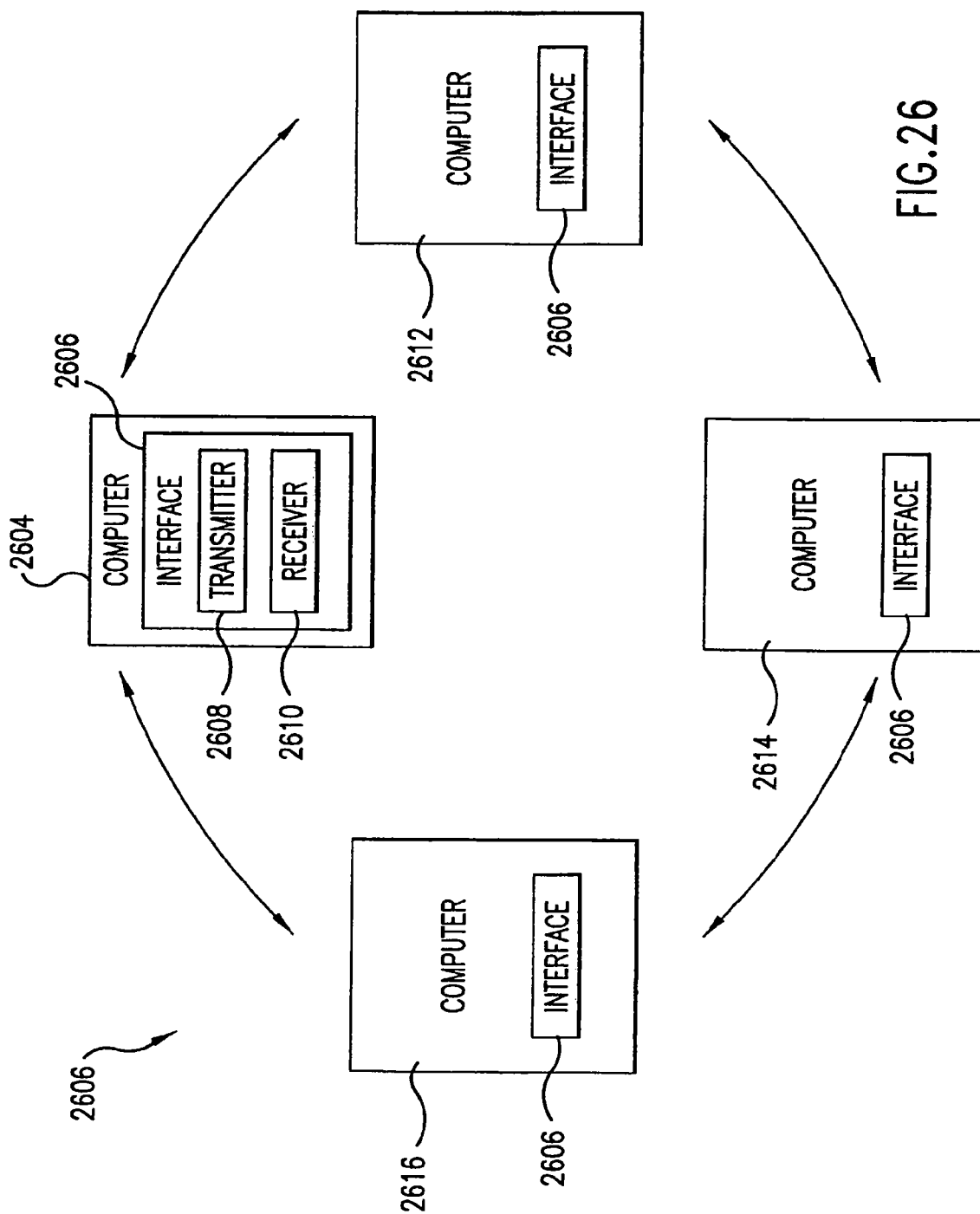


FIG. 25



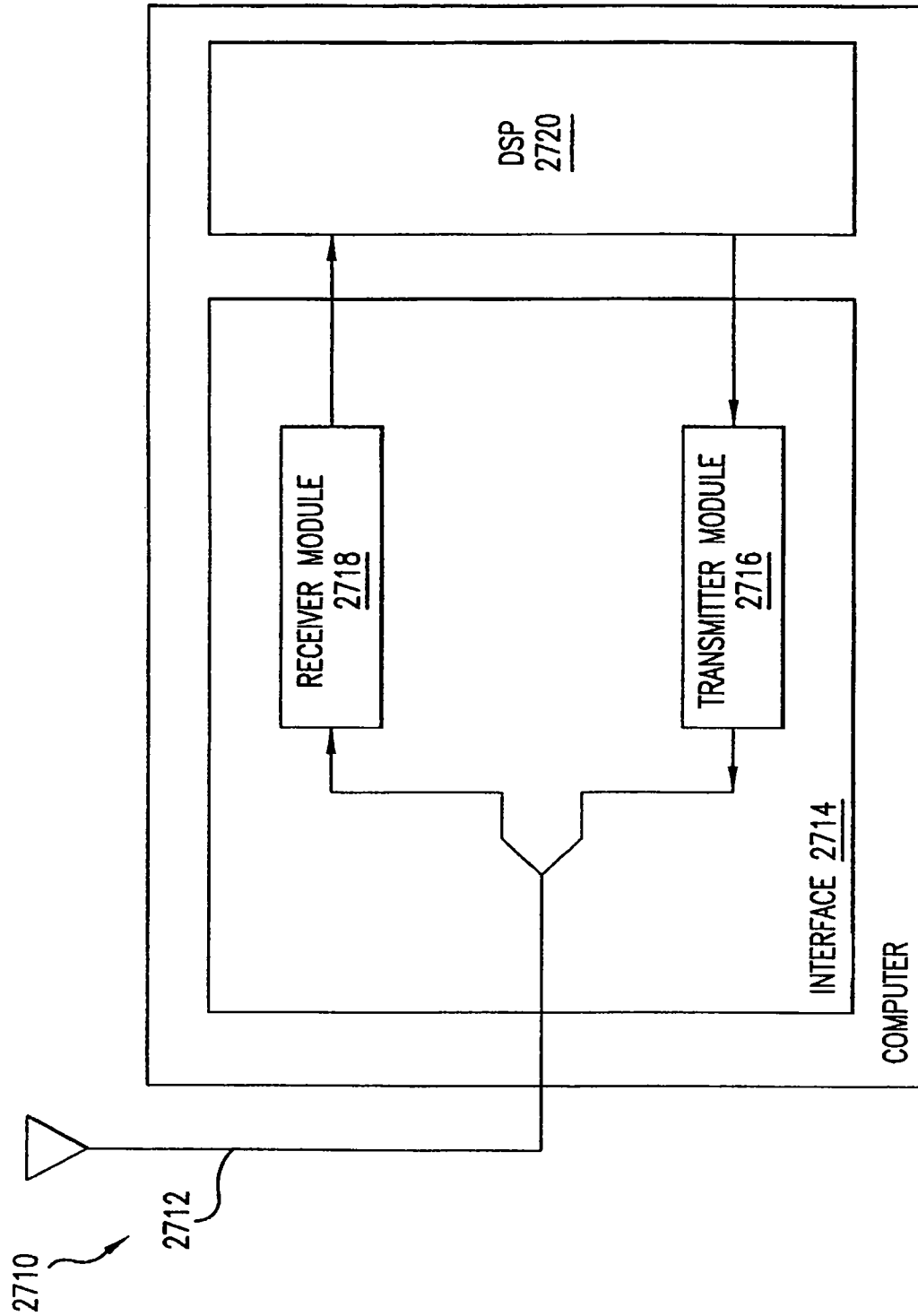


FIG.27

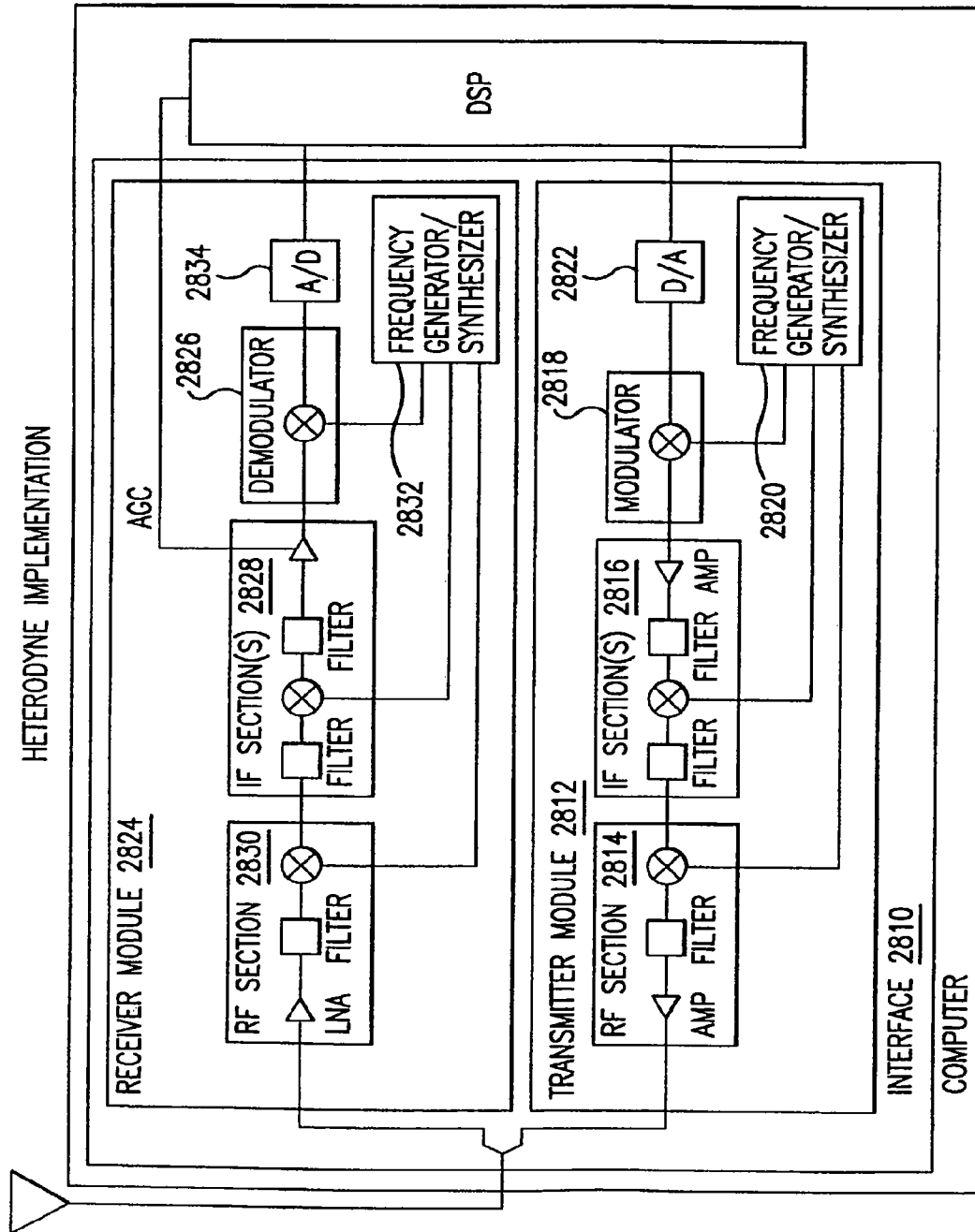
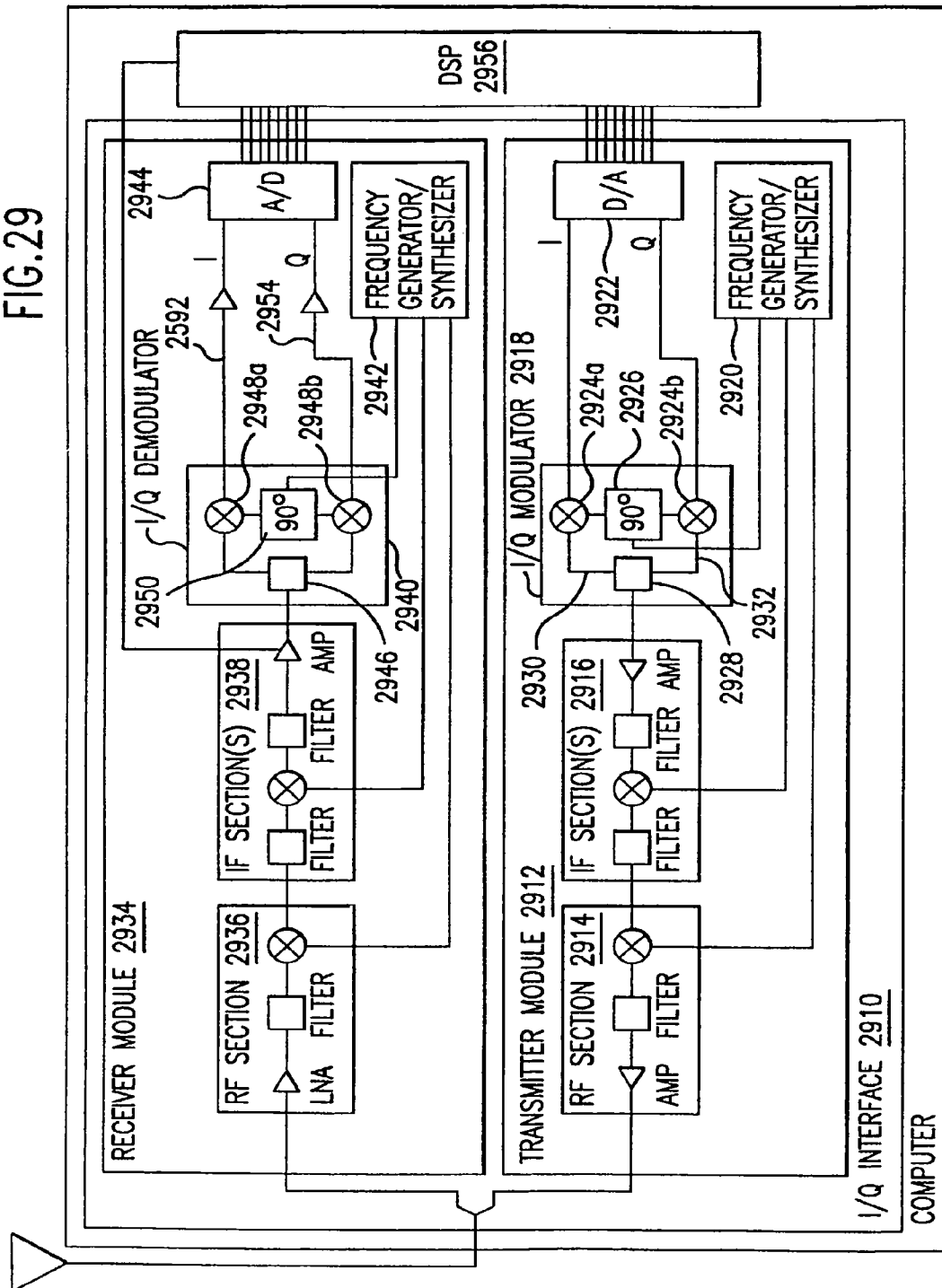


FIG.28

FIG. 29





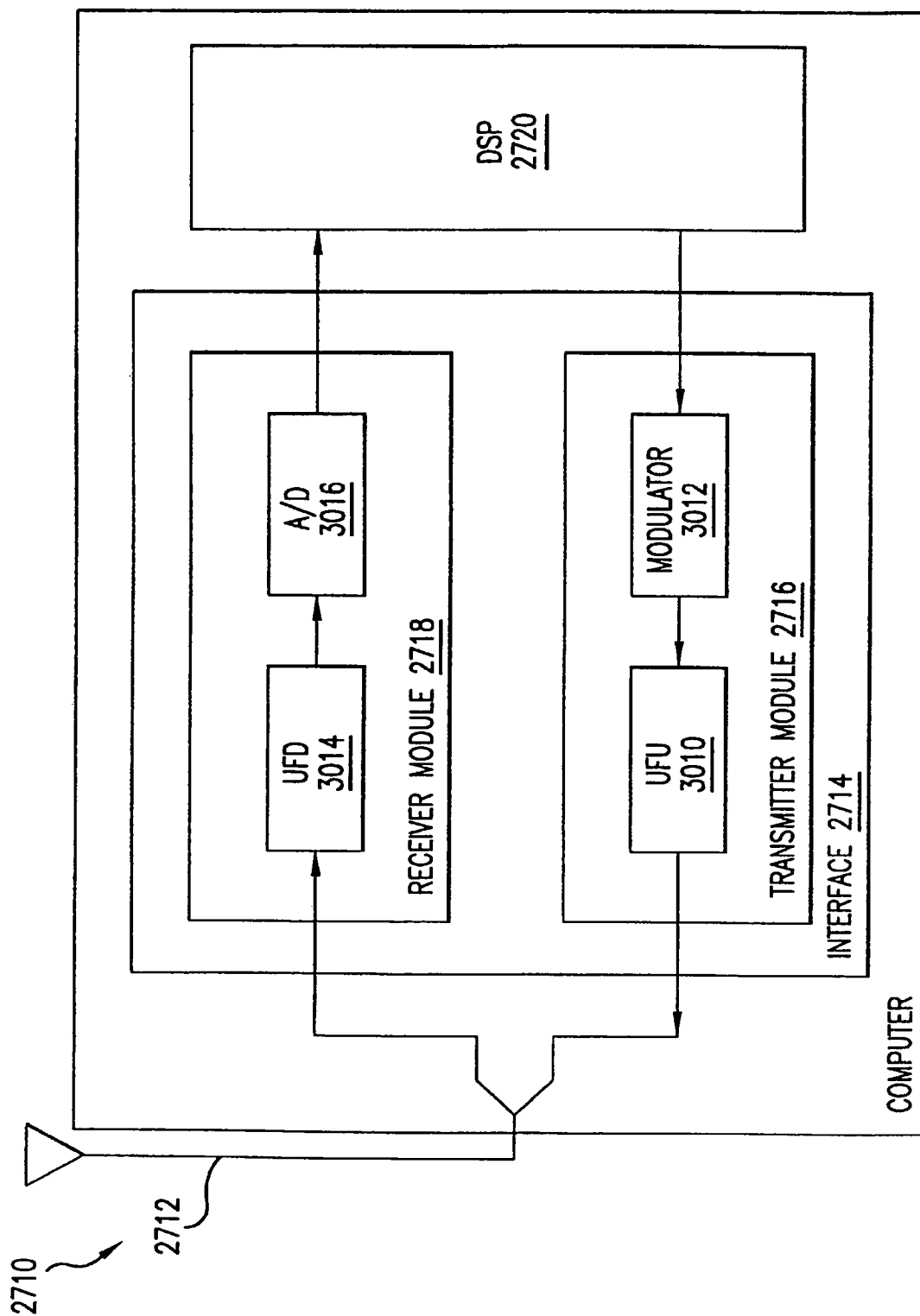


FIG. 30

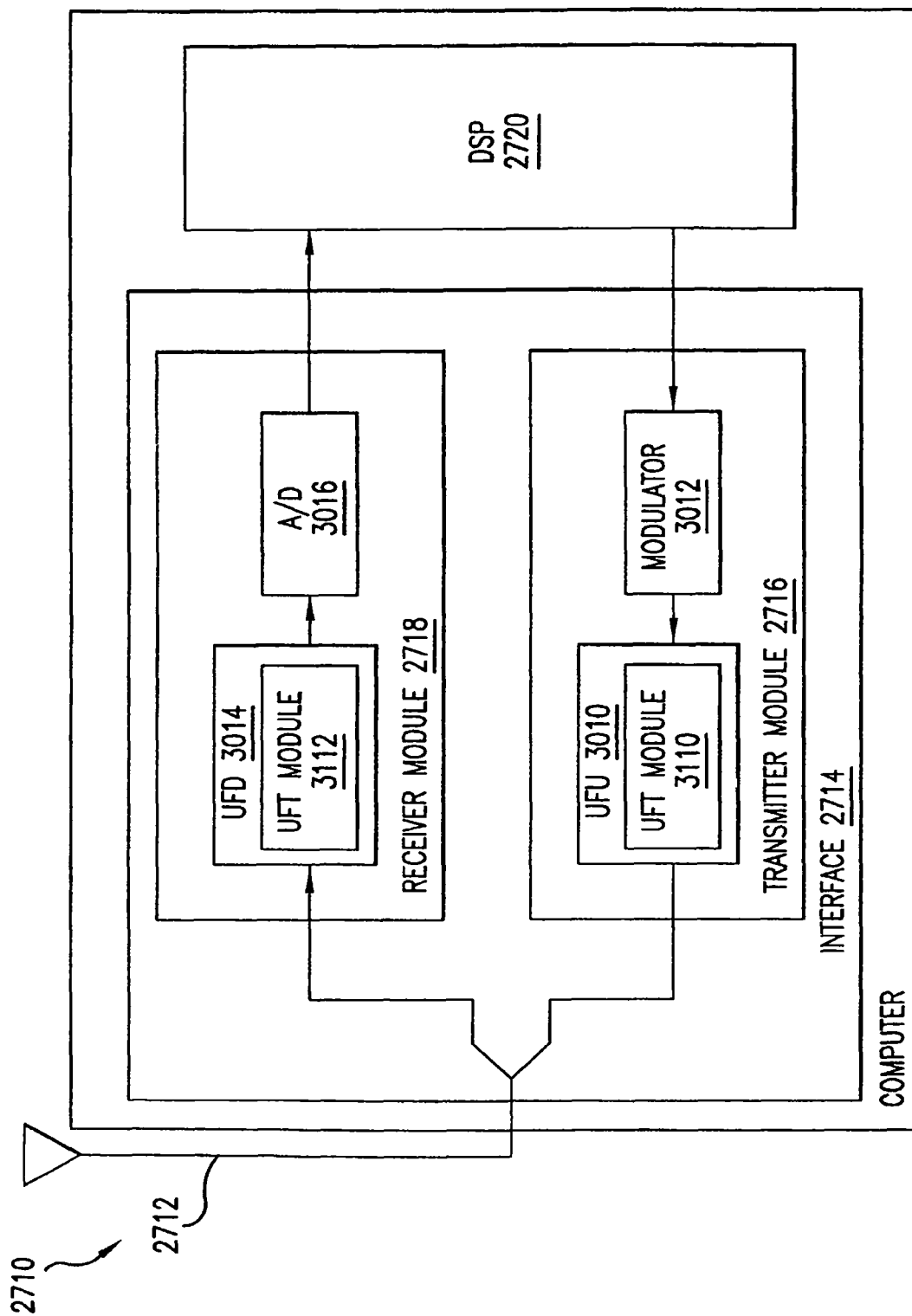


FIG. 31

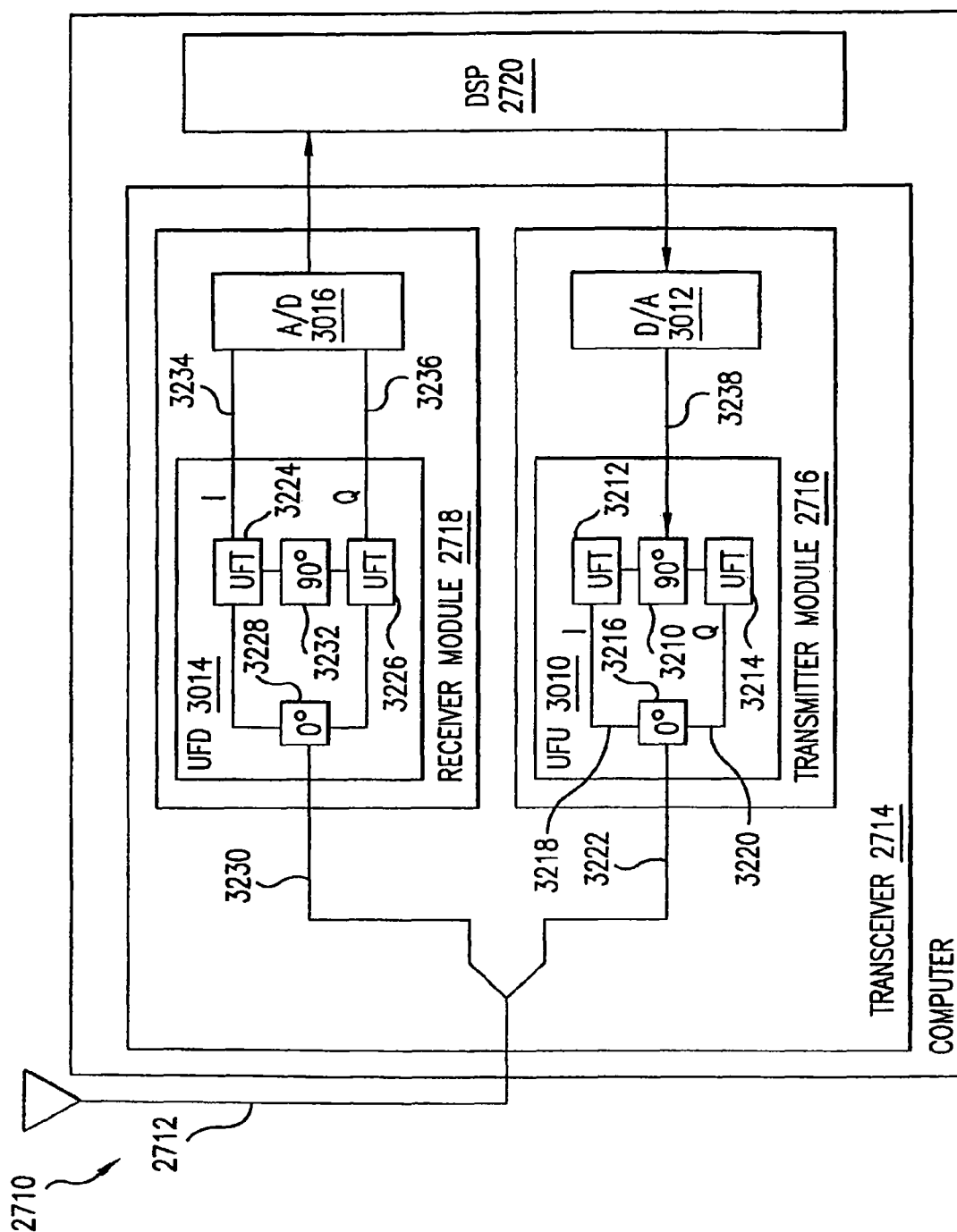


FIG.32

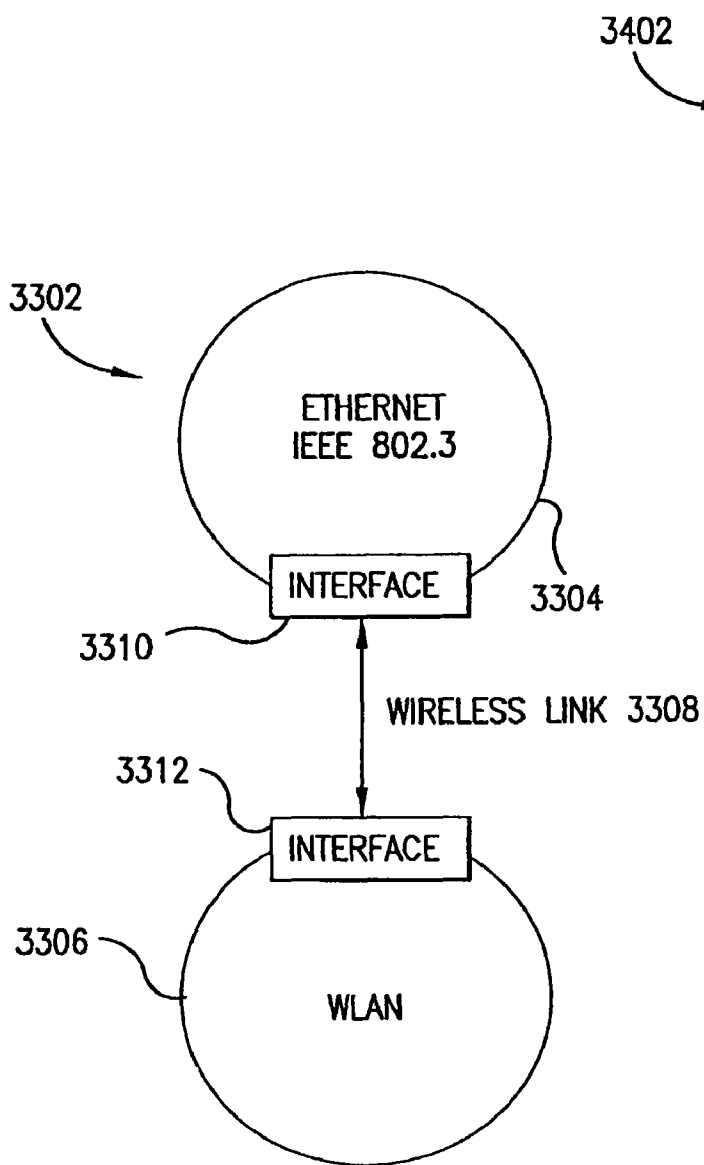


FIG. 33

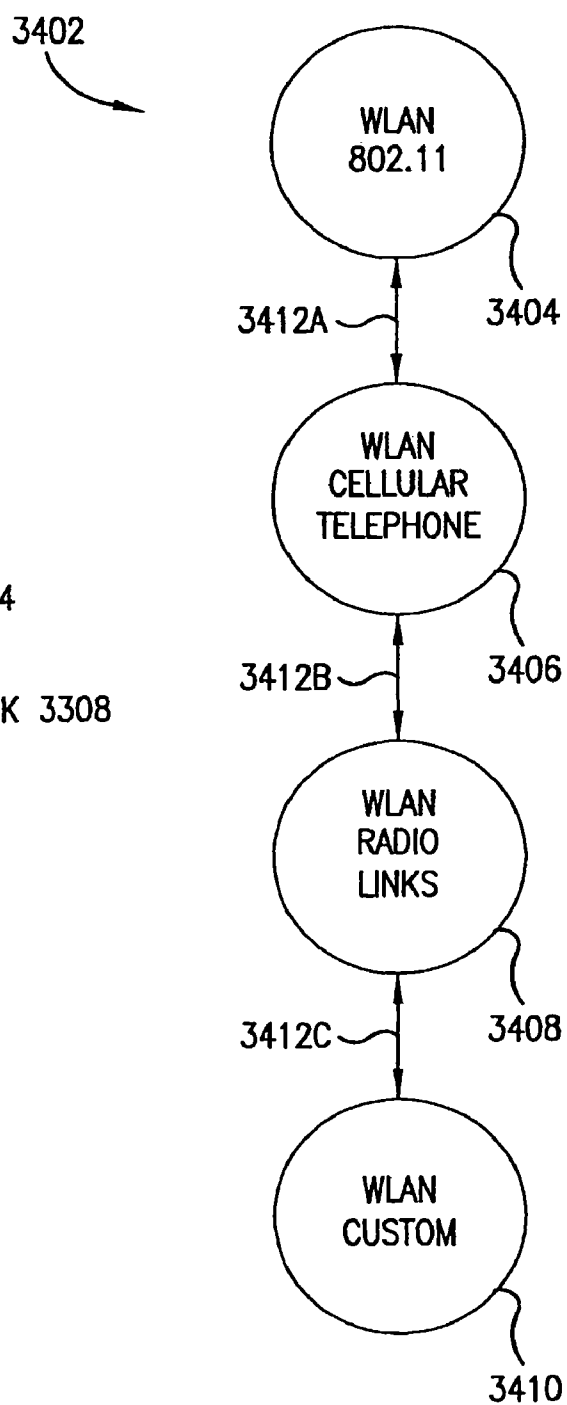


FIG. 34

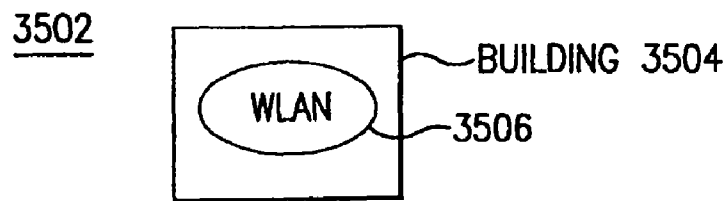


FIG.35

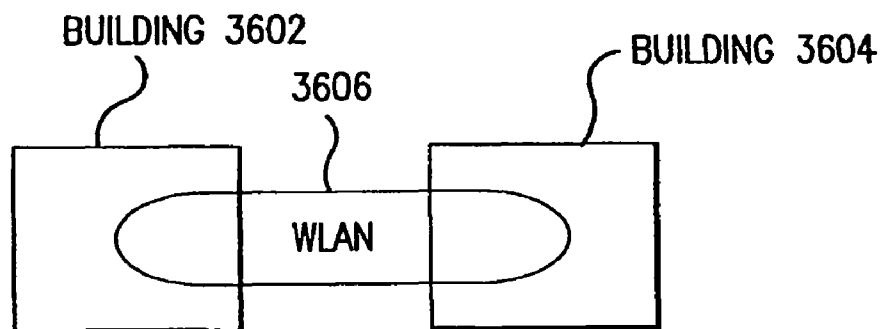


FIG.36

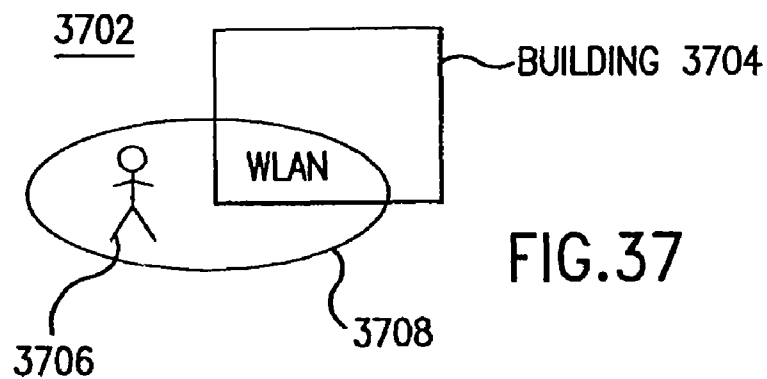


FIG.37

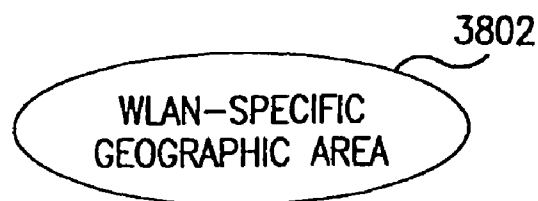


FIG.38

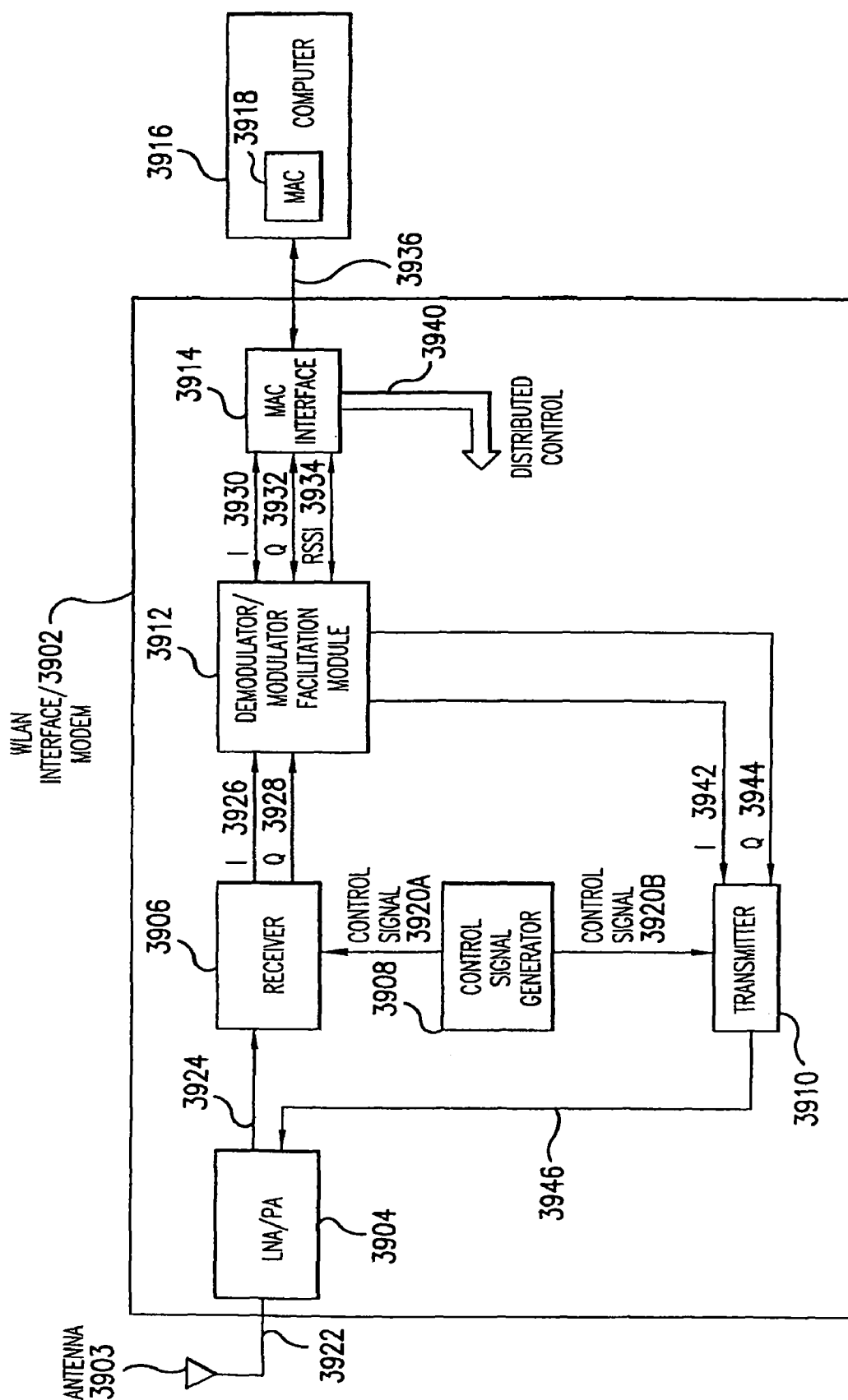


FIG. 39

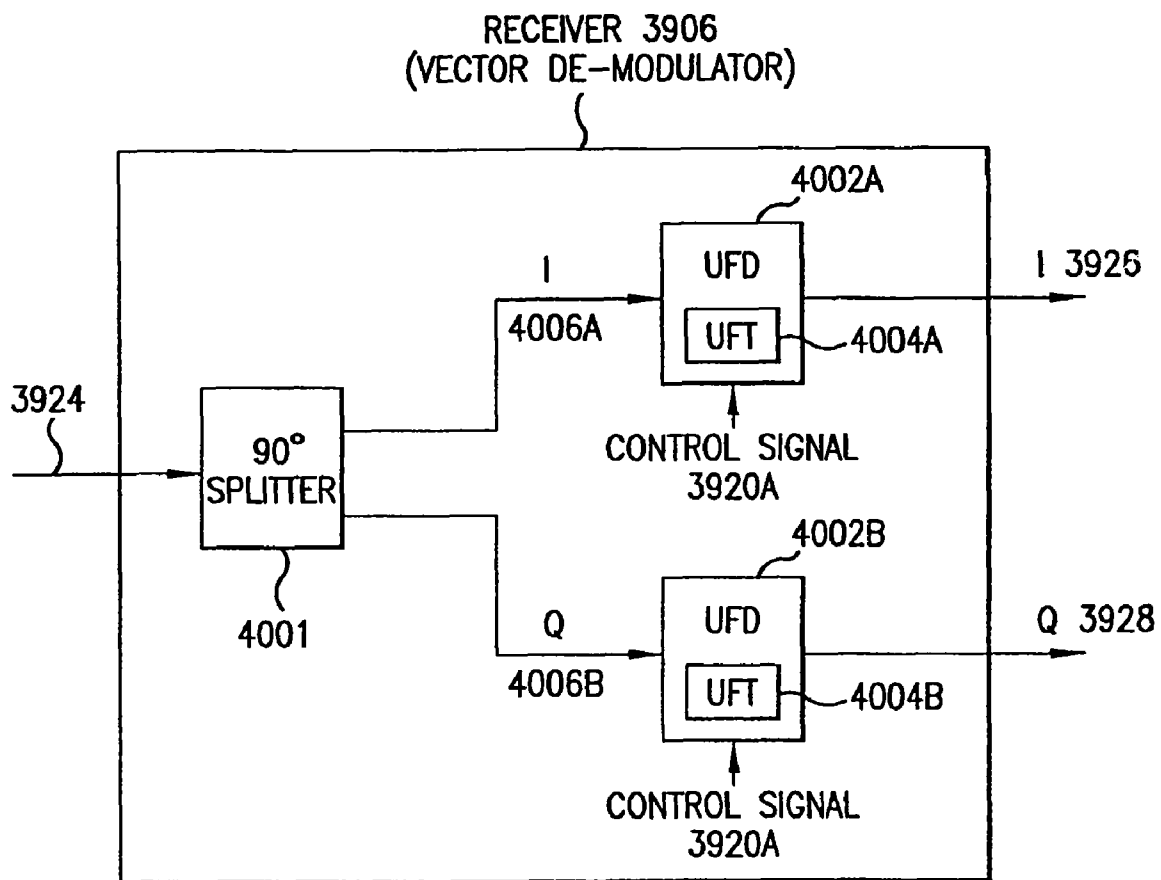


FIG.40

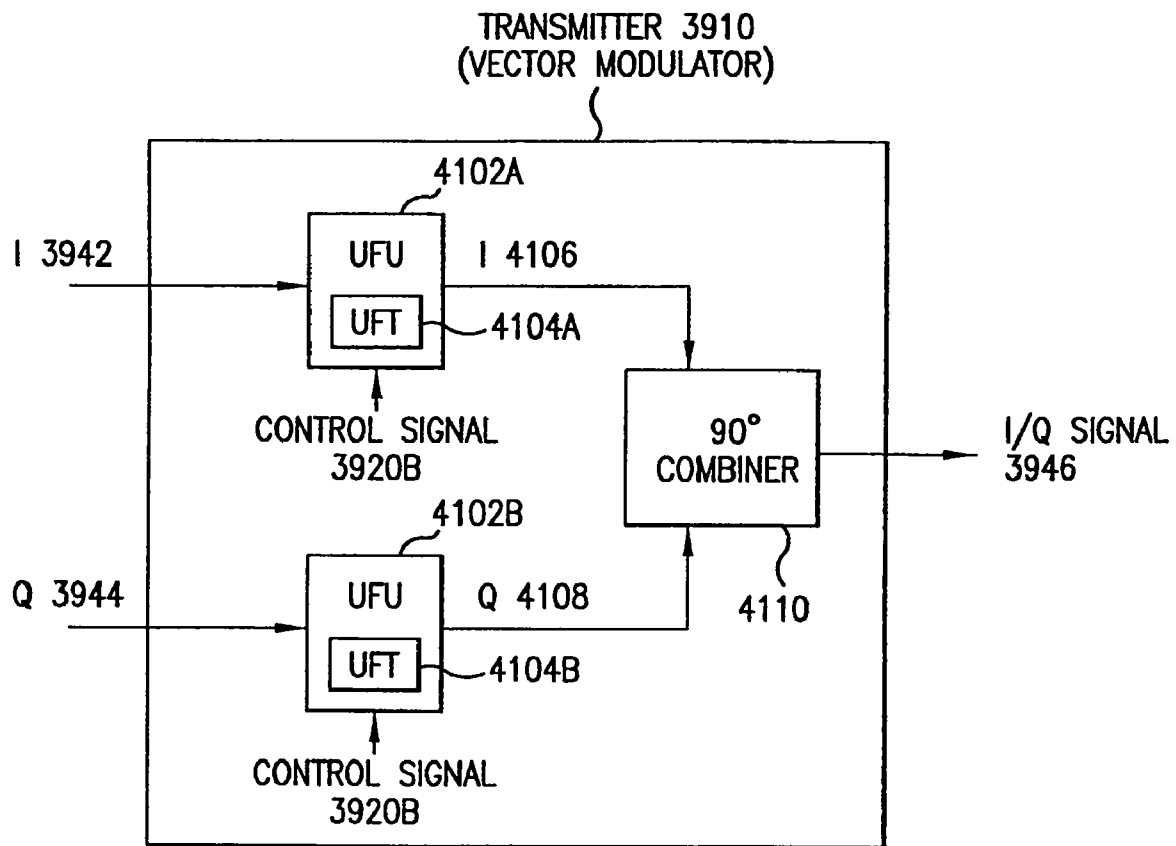
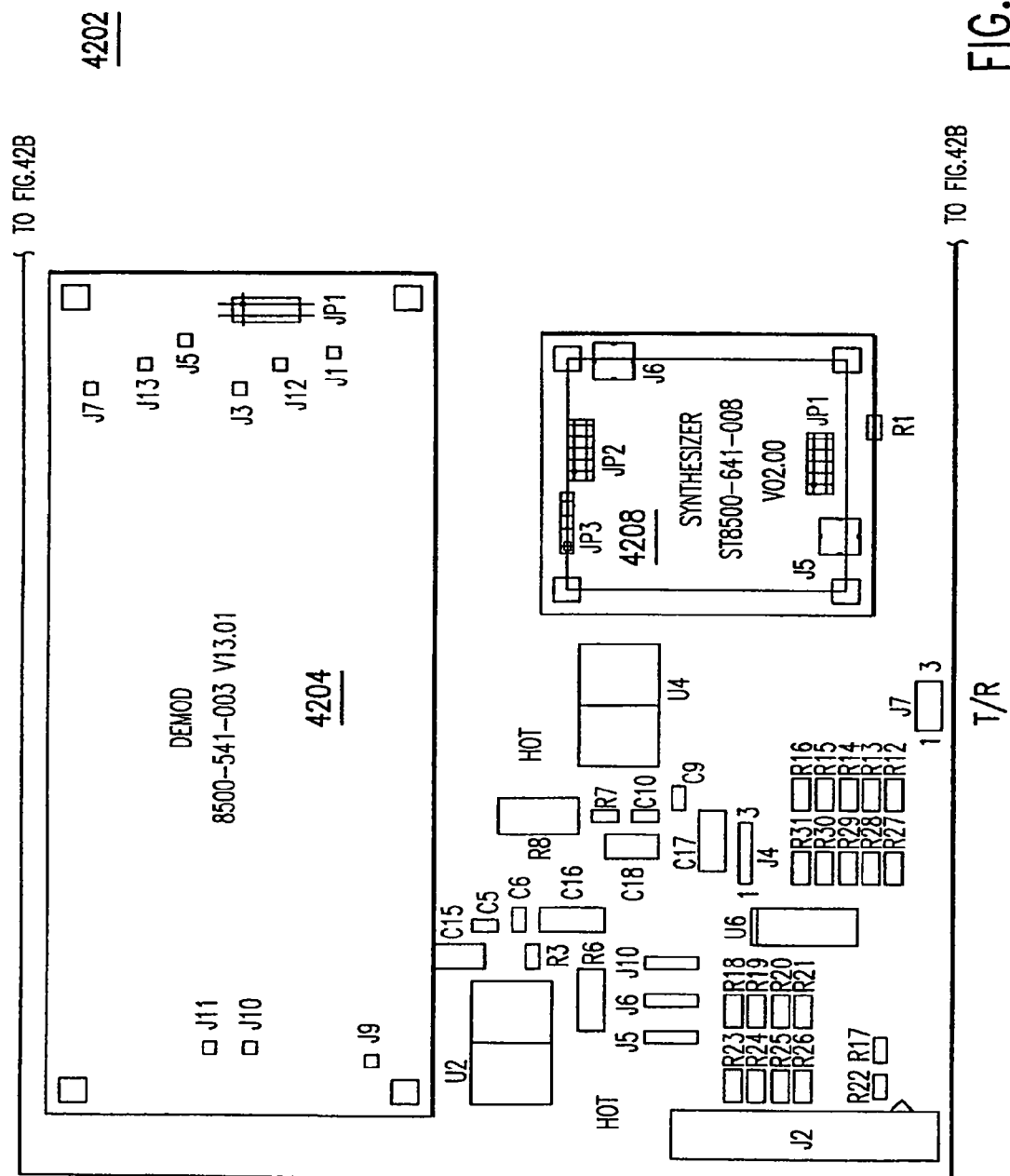
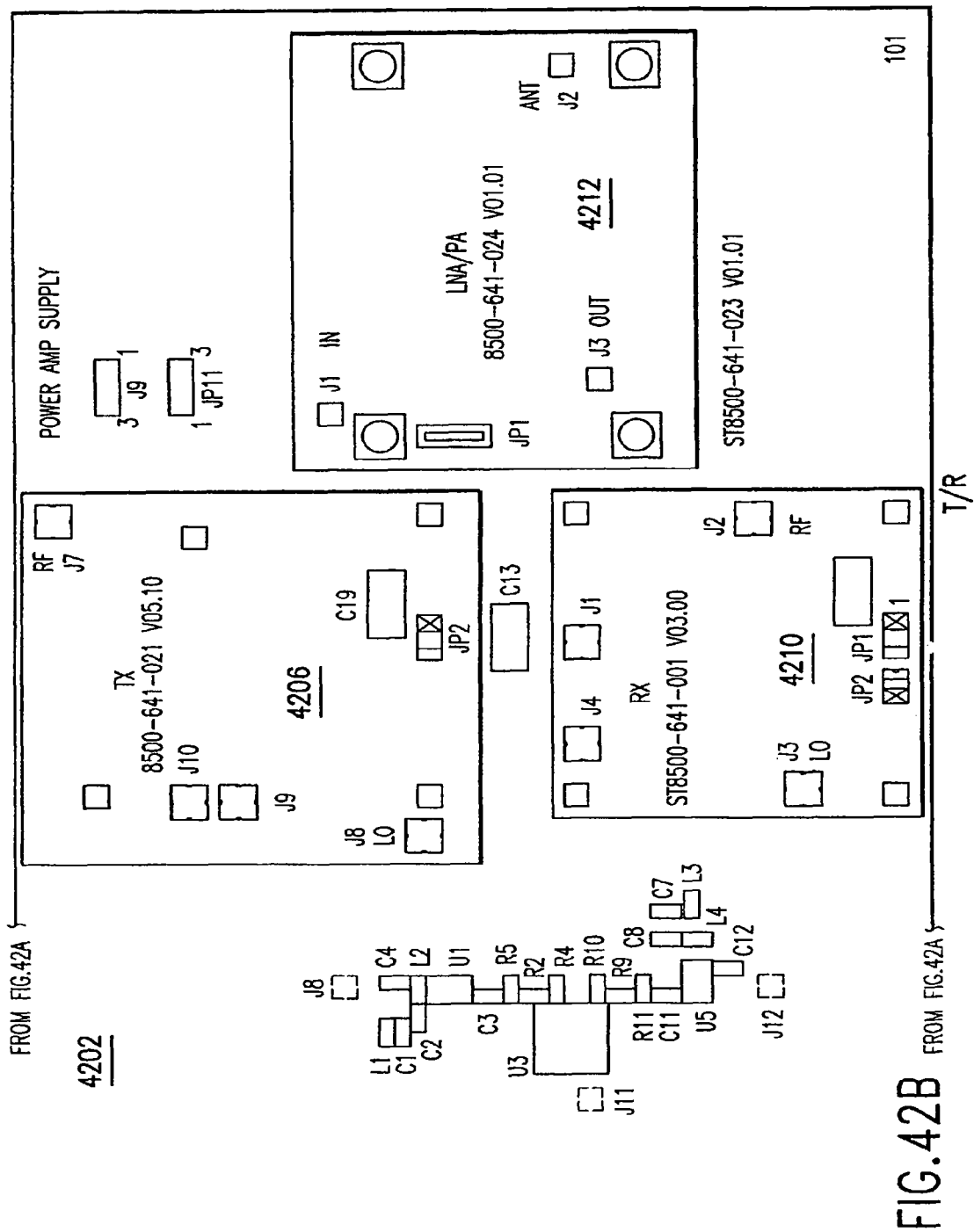


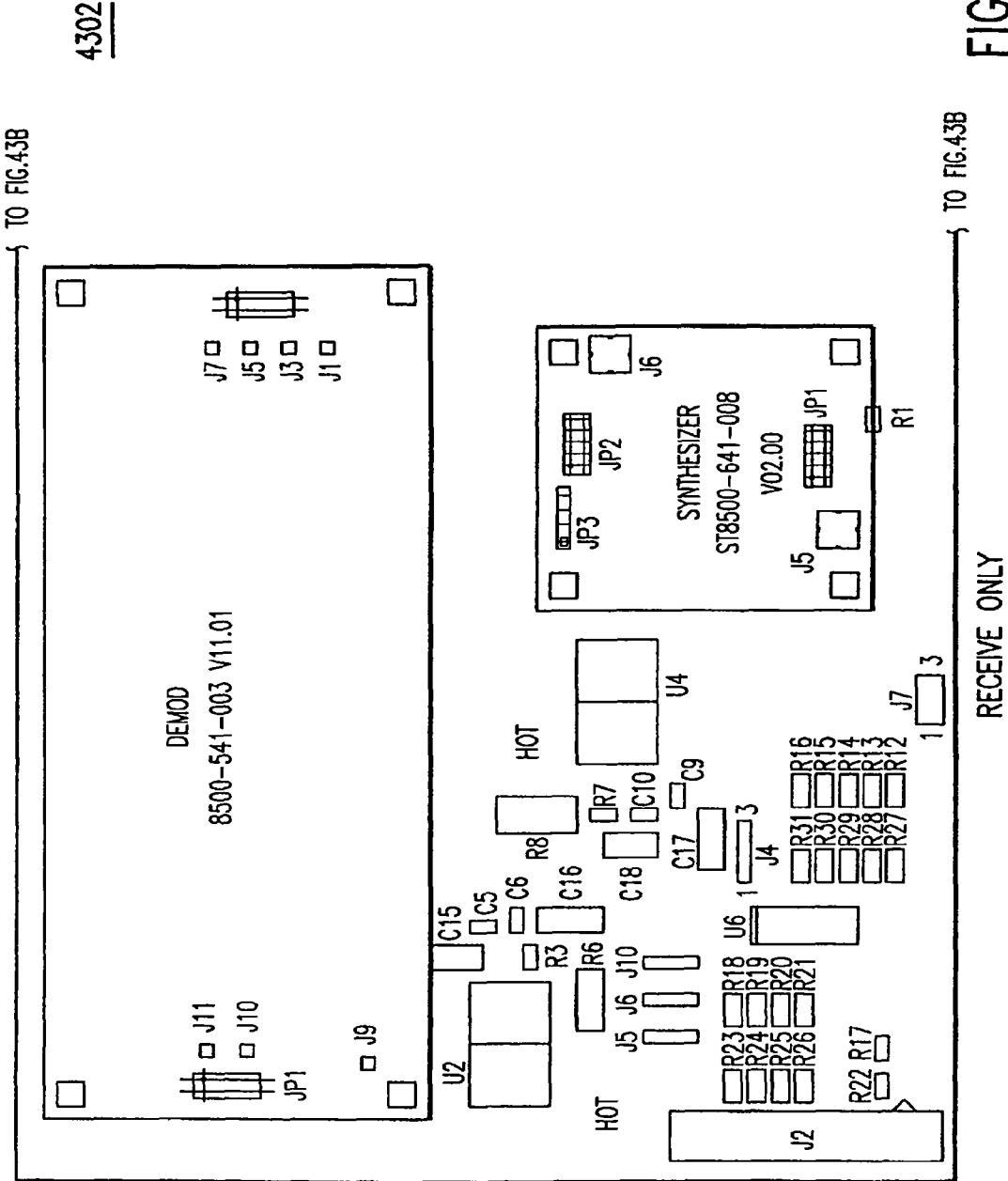
FIG.41

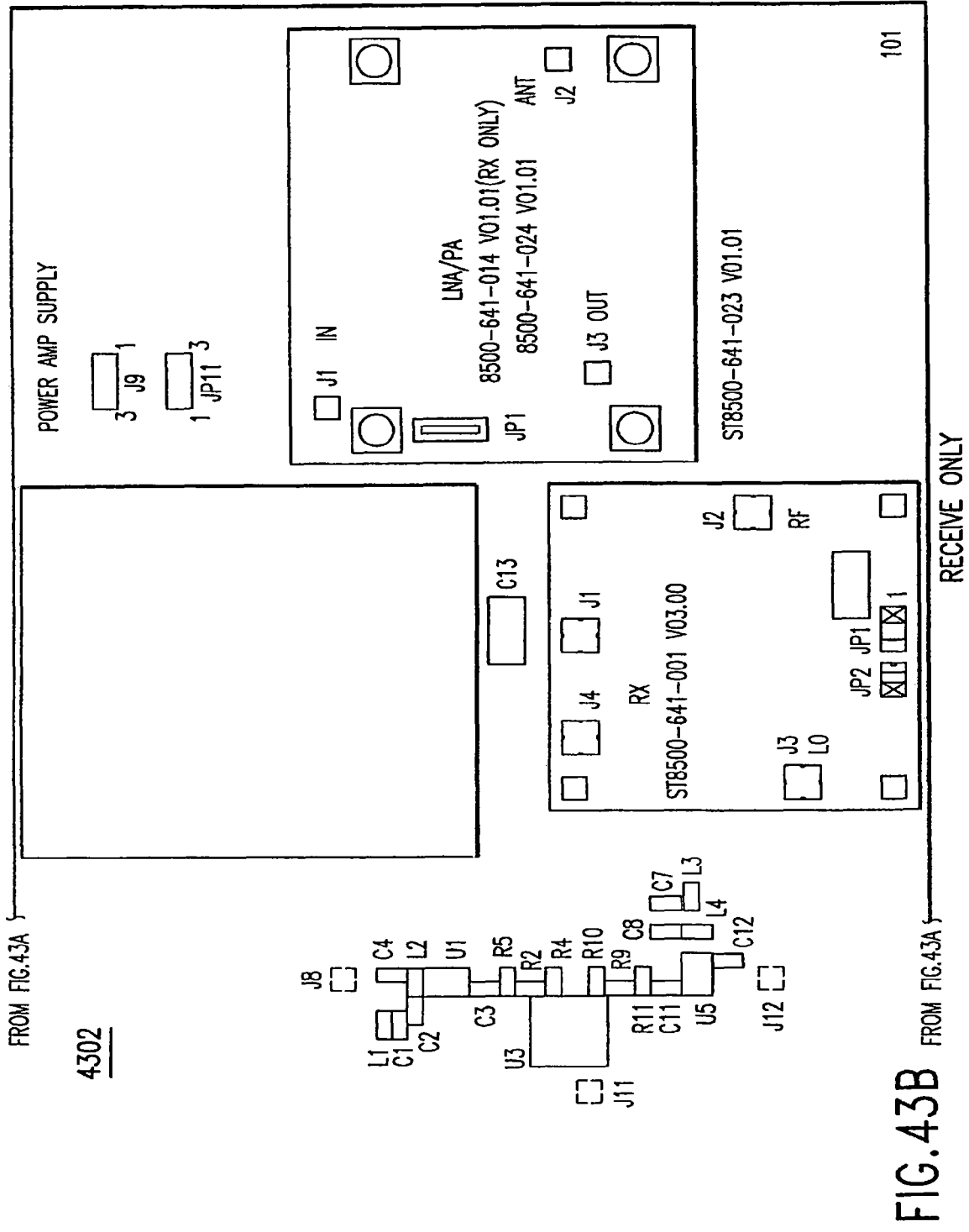


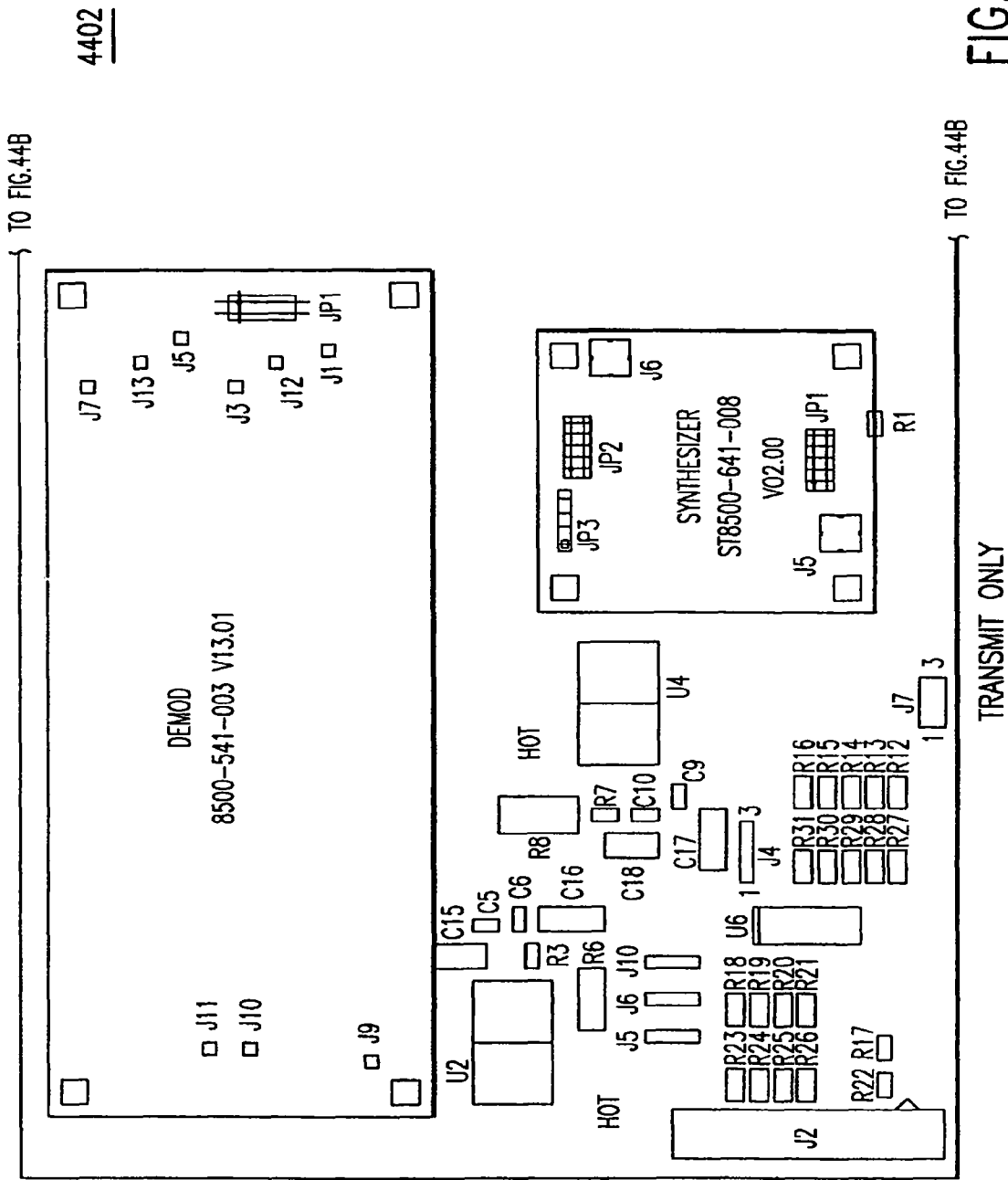


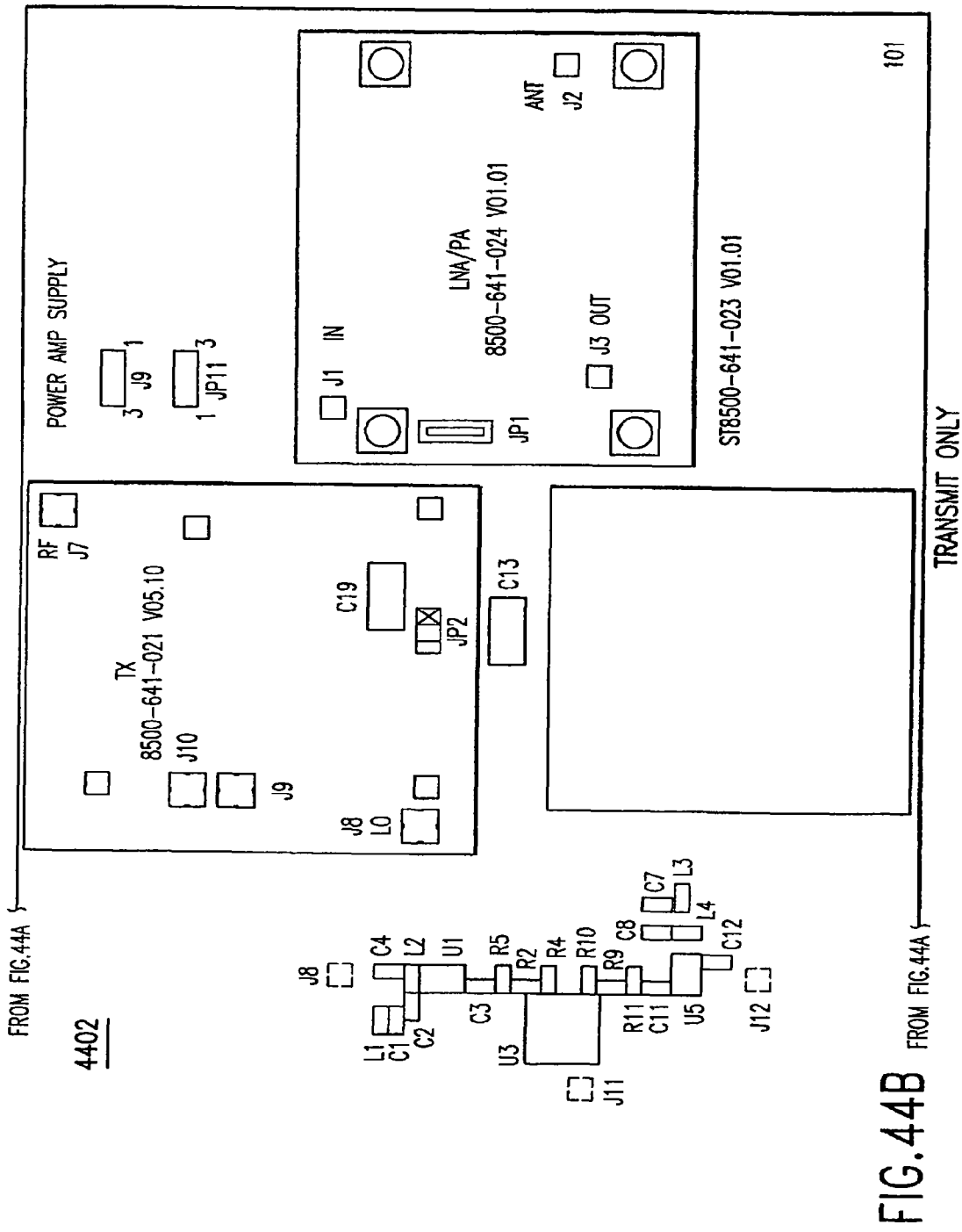
**FIG. 42A**

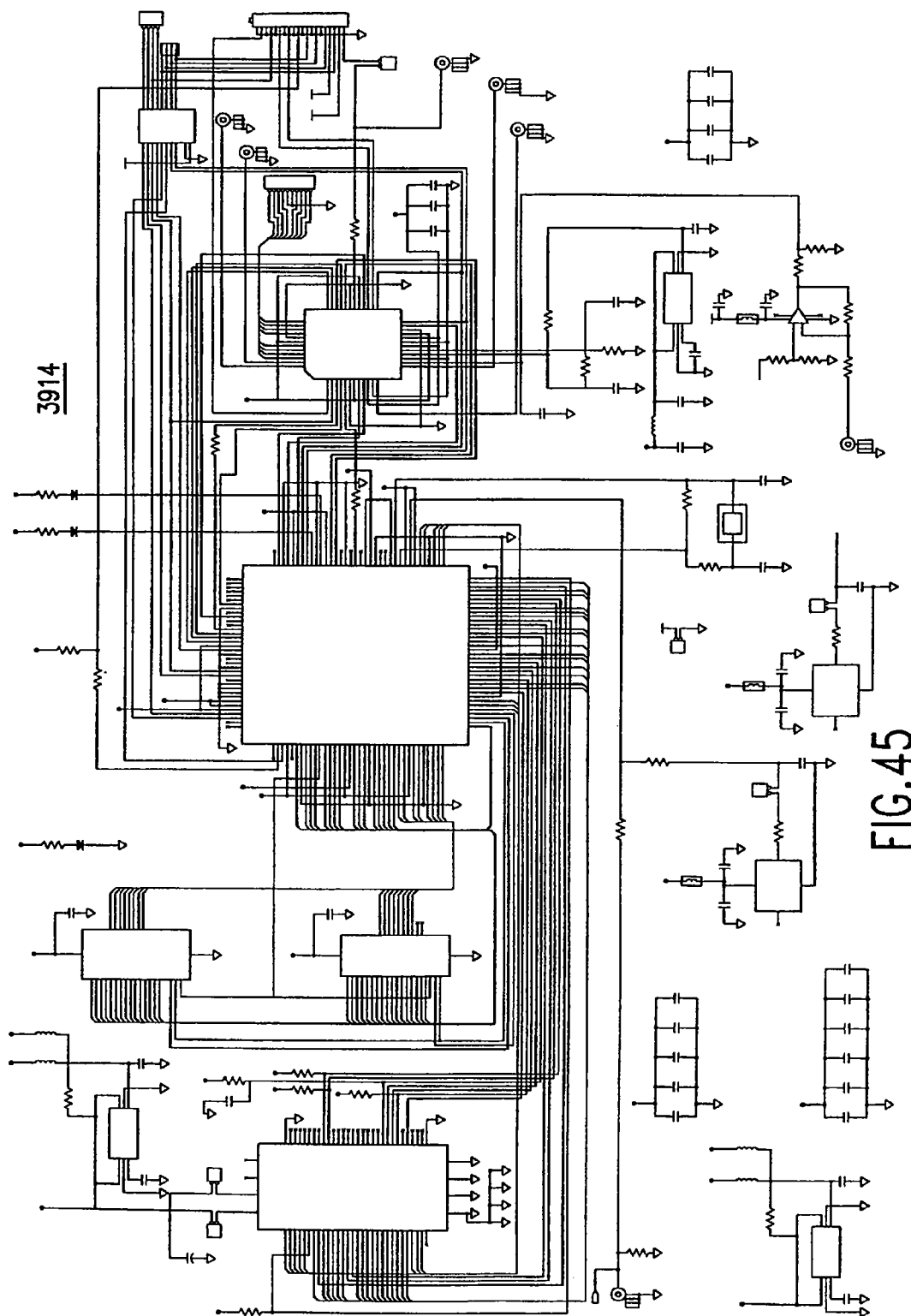












Item	Quantity	Reference	Part Description	Part Number	Manufacturer
1	1	C123	10uF CAP 6032, TANTALUM, 20%	TAJT106K010R	KEMET
2	3	C263, C273, C275, C282	4.7uF CAP 6032, TANTALUM, 20%	T491A475M006AS	KEMET
3	25	C120, C125, C126, C127, C128, C136, C137, C138, C139, C140, C141, C142, C143, C144, C145, C147, C148, C149, C264, C272, C274, C279, C280, C281, C283	0.1uF CAP 0603, X7R, 10%	GRM39X7R104K050AD	MURATA
4	3	C146, C269, C276	.01uF CAP 0603, X7R, 10%	GRM39X7R103K050AD	MURATA
5	5	C124, C132, C133, C271, C278	100pF CAP 0603, X7R, 10%	GRM39C0G101K050AD	MURATA
6	1	C129	47pF CAP 0603, X7R, 10%	GRM39C0G470J100AD	MURATA
7	2	C270, C277	27pF CAP 0603, X7R, 10%	GRM39C0G270K050AD	MURATA
8	1	C130	22pF CAP 0603, X7R, 10%	GRM39C0G220K050AD	MURATA
9	1	C131	10pF CAP 0603, X7R, 10%	GMR39C0G100D050AD	MURATA
10	1	DS1	LED GREEN	597-3311-420	DIALIGHT
11	1	DS2	LED YELLOW	597-3401-420	DIALIGHT
12	1	DS3	LED RED	597-3111-420	DIALIGHT
13	6	JP12, JP13, JP14, JP15, JP16, JP17	CONNECTOR HEADER 2PIN	2MS-19-33-01	SPECIALITY ELECTRONICS
14	1	JP11	CONNECTOR HEADER 4PIN	100/VH/TM1SQ/W.100/4	BLKCON

FIG.46A



15	7	J16, J20, J21, J22, J23, J24, J25	CONNECTOR 82MCMX	82MCMX-50-0-1	HUBER/SHUNER
16	1	J18	CONNECTOR HEADER 10	TMS-110-01-G-S	SAMTEC
17	1	J19	CONNECTOR WITH EJECTOR	EHT-1-10-01-S-D	SAMTEC
18	1	P1	CONNECTOR 34X2POMCIA	D10MJ-68S-SPC-M08	ITT CANON
19	7	L59, L60, L61, L63, L64, L65, L66	FERRITE BEAD	BLM11A121S	MURATA
20					
21	1	R112	10M, RESISTOR, 0603, 5%	ERJ-3GSYJ394V	PANASONIC
22	1	R114	390K, RESISTOR, 0603, 5%	ERJ-3GSYJ104V	PANASONIC
23	1	R105	100K, RESISTOR, 0603, 5%	ERJ-3GSYJ153V	PANASONIC
24	4	R106, R107, R108, R111	15K, RESISTOR, 0603, 5%	ERJ-3GSYJ912V	PANASONIC
25	1	R116	9.1K, RESISTOR, 0603, 5%	ERJ-3GSYJ822V	PANASONIC
26	1	R115	8.2K, RESISTOR, 0603, 5%	ERJ-3GSYJ392V	PANASONIC
27	1	R113	3.9K, RESISTOR, 0603, 5%	ERJ-3GSYJ751V	PANASONIC
28	1	R101	750, RESISTOR, 0630, 5%	ERJ-3GSYJ561V	PANASONIC
29	1	R110	560, RESISTOR, 0603, 5%	ERJ-3GSYJ331V	PANASONIC
30	2	R99, R100	330, RESISTOR, 0603, 5%	ERJ-3GSYJ500V	PANASONIC
31	1	R119	50, RESISTOR, 0603, 5%	ERJ-3GSYJ100V	PANASONIC
32	2	R128, R129	10, RESISTOR, 0603, 5%	RM732Z1J000ZT	ERJ KOA
33	8	R102, R103, R104, R109, R117, R118, R120, R127, R121, R122, R123, R124, R125, R126	0, RESISTOR, 0603, 5%	3GSYJ000V	PANASONIC
34	6		TBD, RESISTOR, 0603, 5%	R	PANASONIC
35	1	U10	SRAM	K1M62256DL TG-5L	SAMSUNG
36	1	U12	MAC	M5M5256CVP-55LL AM79C930	MITSUBUSHI AMD

FIG. 46B

37	1	U13	BASEBAND PROCESSOR	HFA3842A1	HARRIS
38	1	U14	FLASH RAM	AM29F010-55EC	AMD
39	1	U15	32 KHz CRYSTAL	CX-6V-SM2-32.768KHzC/1	STATEK
40	2	U45	BUS BUFFER	DS3862	NATIONAL
41	1	U48	REGULATOR 3.5 V	TK11235BMC	TOKO
42	1	U49	22MHz OSCILLATOR	FOX F3346-22MHz	FOX
43	1	U50	2 VOLT REFERENCE	TK11220BMC	TOKO
44	1	U51	40MHz OSCILLATOR	CXO-M-10N-40MHz A/1	STATEK

FIG.46C

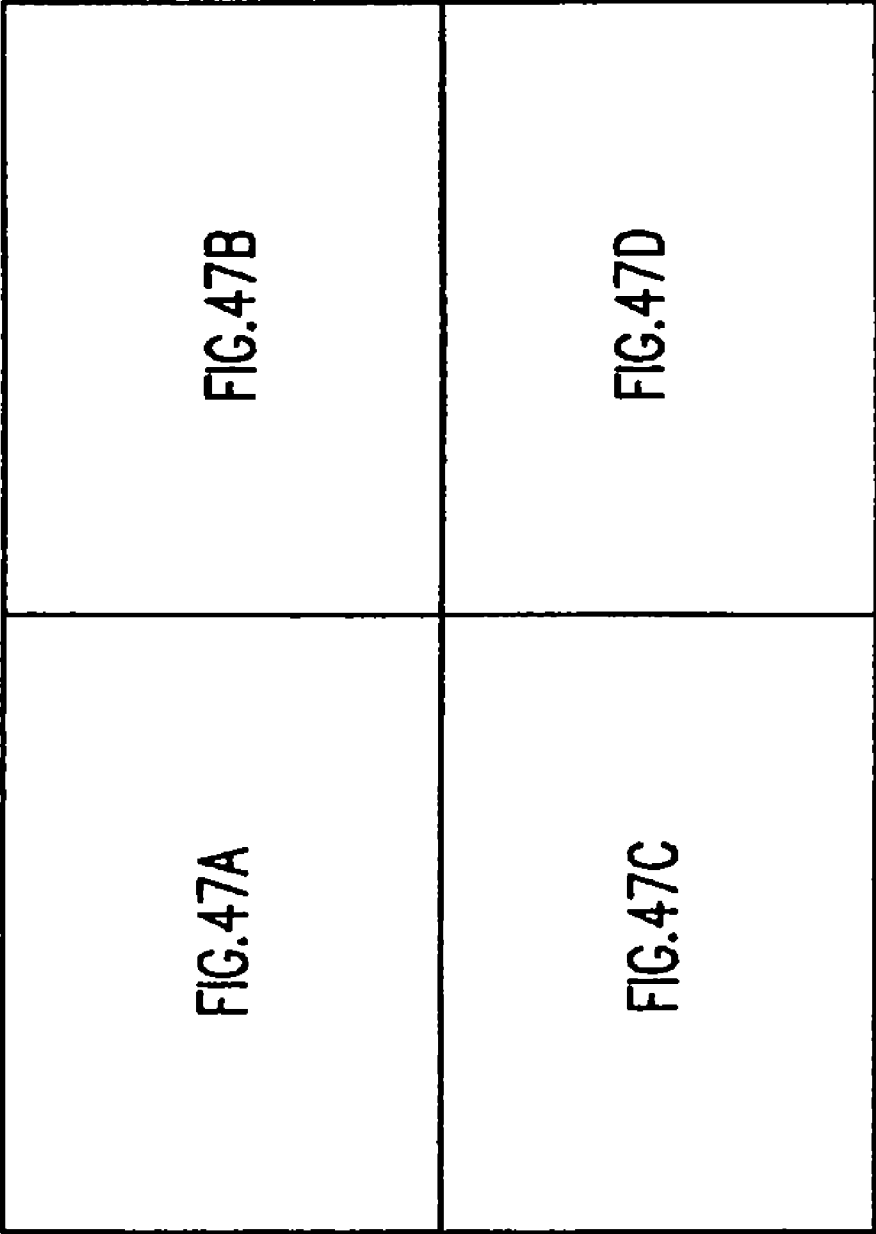
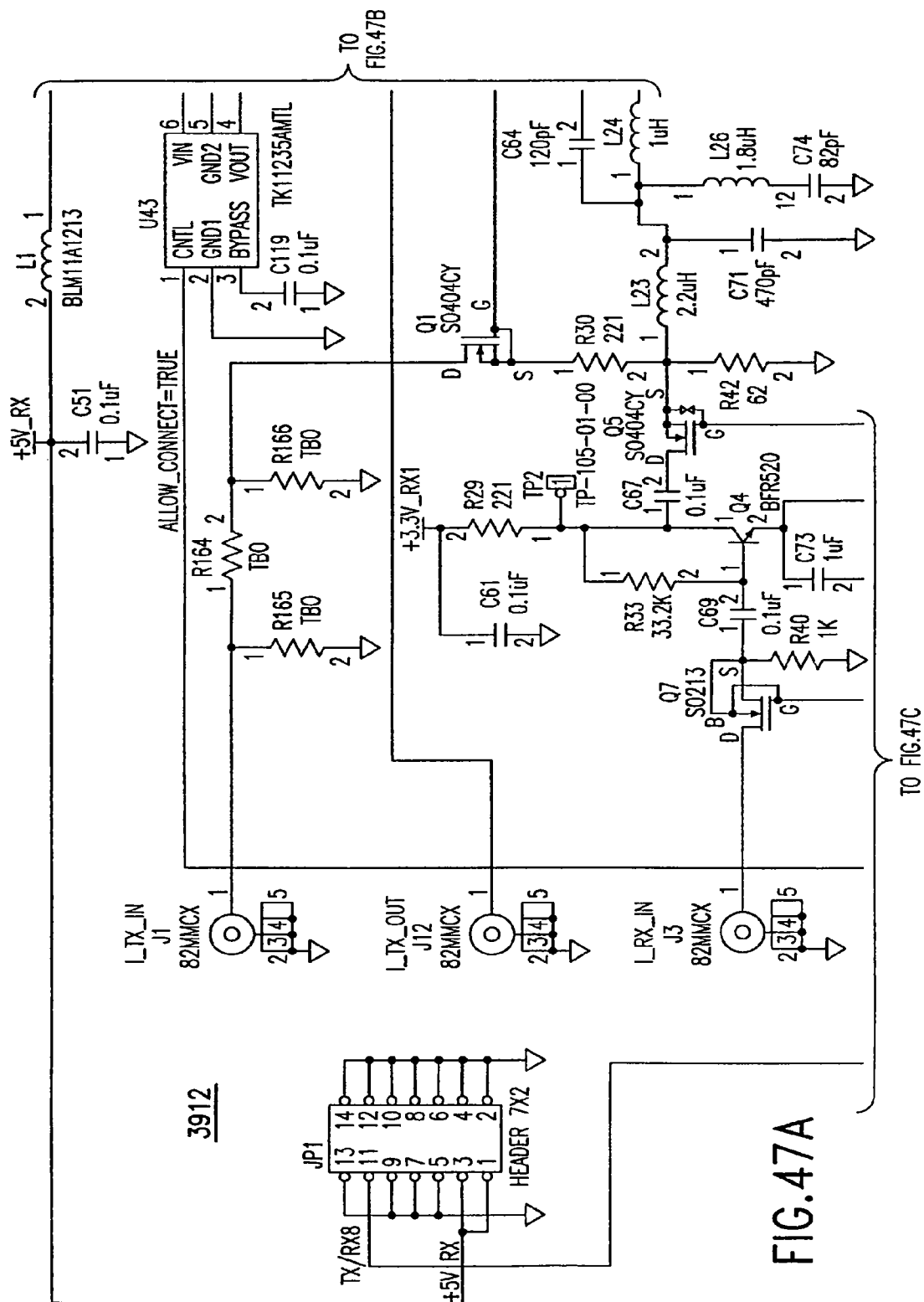
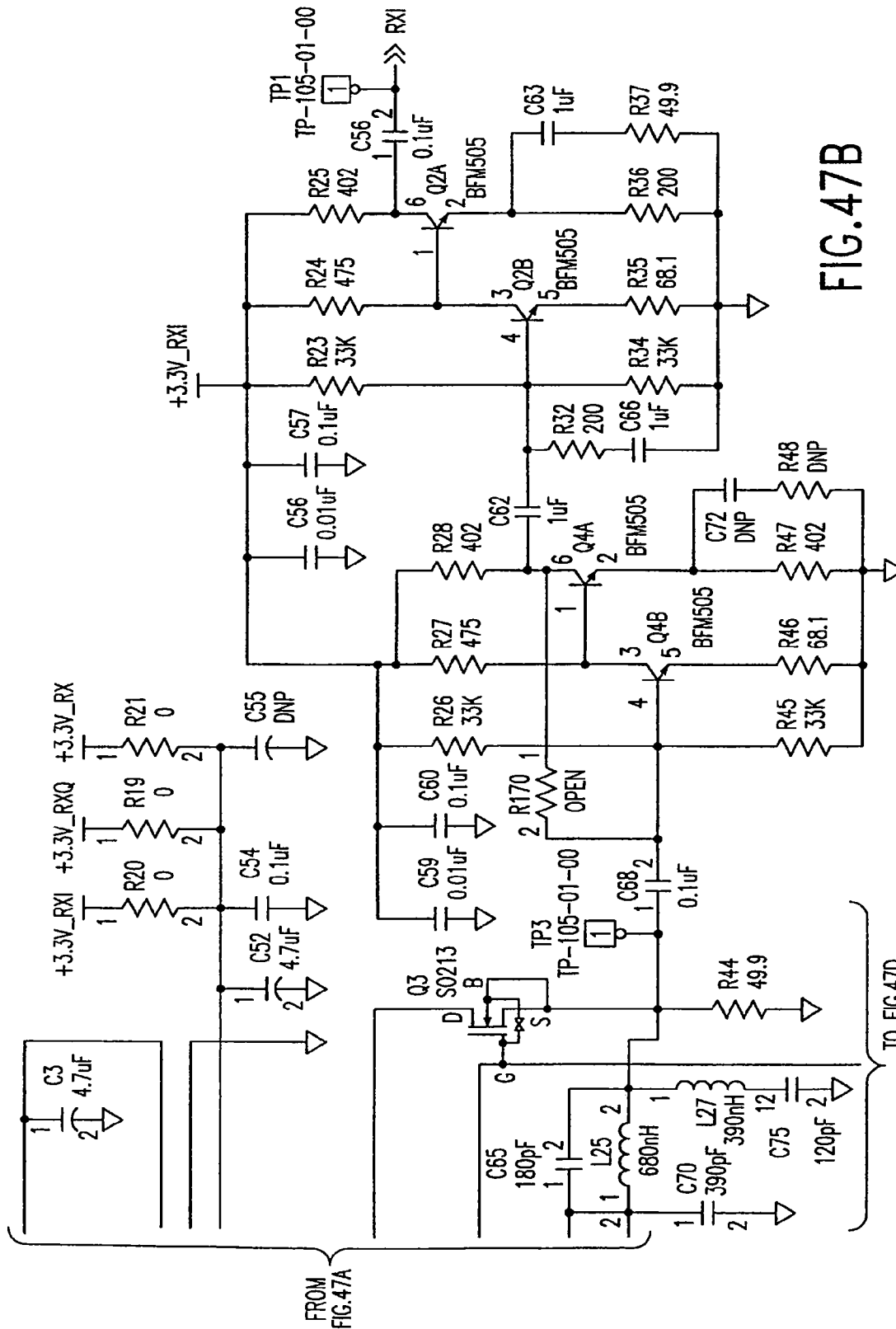
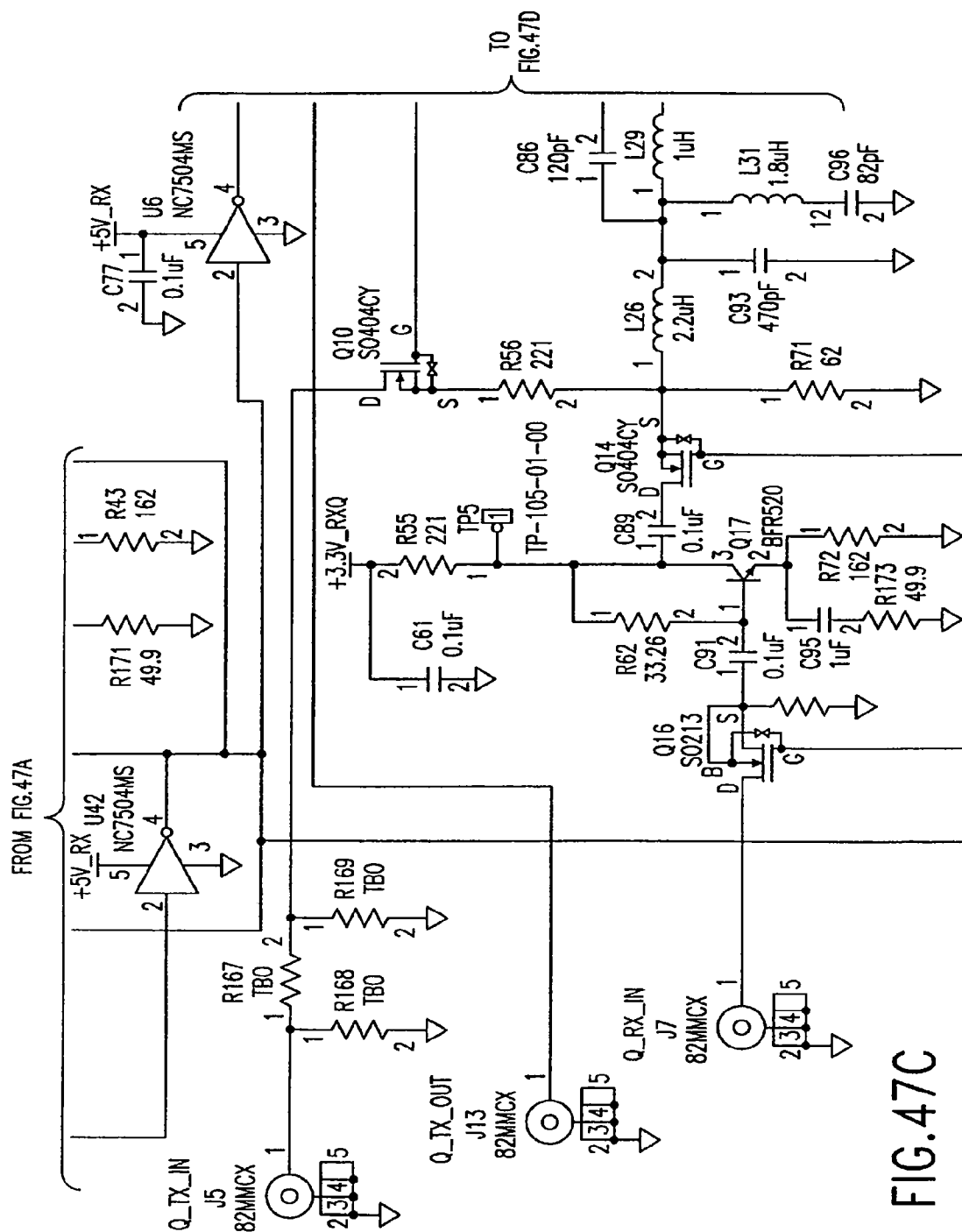
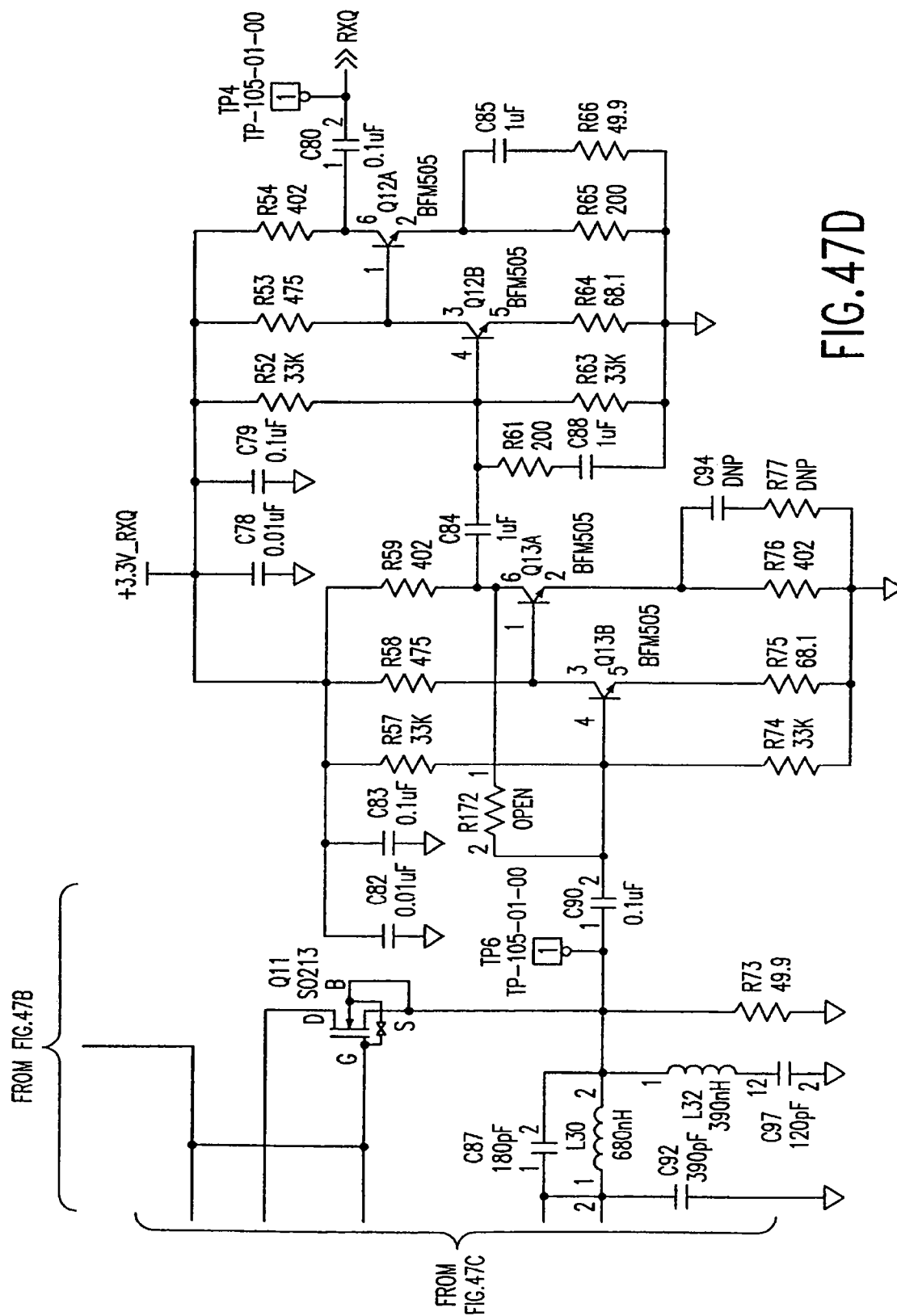


FIG. 47









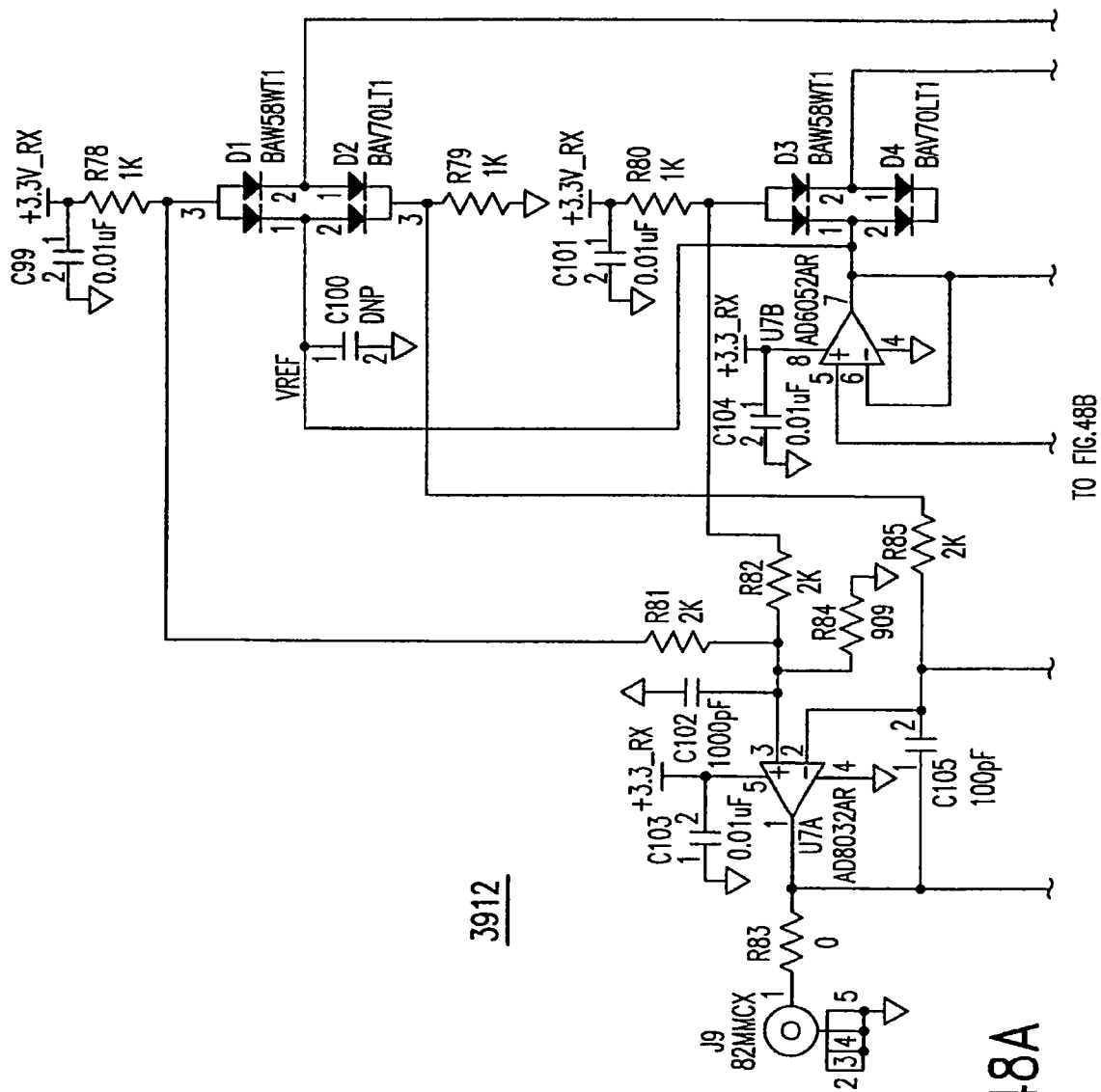


FIG. 48A



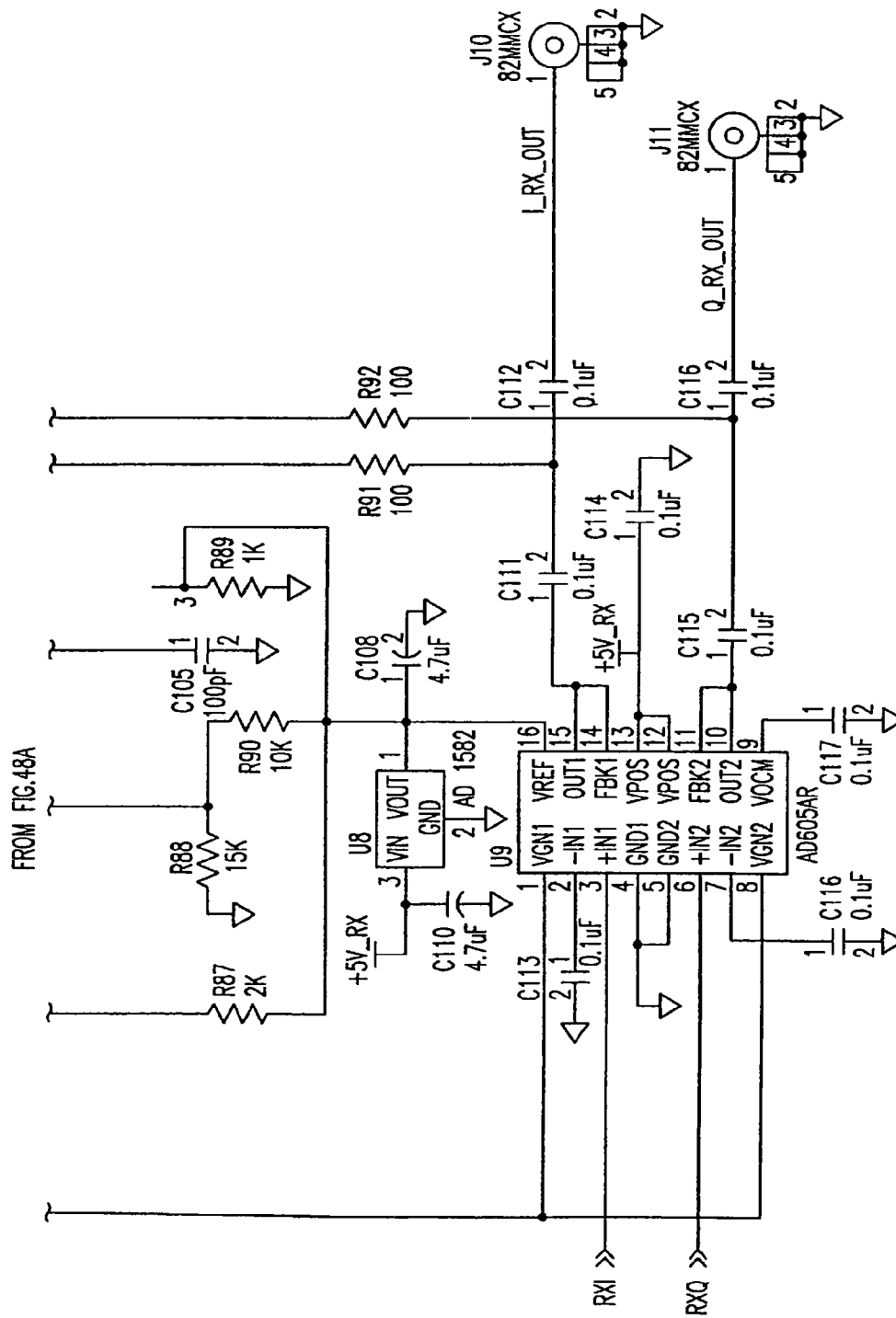


FIG. 48B

ITEM	QUANT.	REFERENCE	PART	PART NUMBER	MANUFACTURER
1	4	C3, C52, C108, C110	4.7uF	T491A475K006AS	KEMET
2	26	C51, C54, C57, C58, C60, C61, C67, C68, C69, C77, C79, C80, C81, C83, C89, C90, C91, C111, C112, C113, C114, C115, C116, C117, C118, C119	0.1uF	GRM39Y5V104Z016	MURATA
3	1	C55	DNP	T491A475K006AS	KEMET
4	8	C56, C59, C78, C82, C99, C101, C103, C104	0.01uF	GRM39X7R103K050	MURATA
5	8	C62, C63, C66, C73, C84, C85, C88, C95	1uF	GRM40Y5V105Z016	MURATA
6	4	C64, C75, C86, C97	120pF	GRM39CCG121J050	MURATA
7	2	C65, C87	180pF	GRM39CCG181J050	MURATA
8	2	C70, C92	390pF	GRM39CCG391J050	MURATA
9	2	C71, C93	470pF	GRM39CCG471J050	MURATA
10	2	C72, C94	DNP	GRM40Y5V105Z016	MURATA
11	2	C74, C96	82pF	GRM39CCG820J050	MURATA
12	2	C100, C106	DNP	DNP	MURATA
13	2	C105, C102	1000pF	GRM39CCG102K050	MURATA
14	2	D3, D1	BAW56WT1	BAW56WT1	MOTOROLA
15	2	D4, D2	BAV70LT1	BAV70LT1	MOTOROLA
16	1	JP1	HEADER 7X2	FTSH-107-02-L-D	SAMTEC
17	9	J1, J3, J5, J7, J9, J10, J11, J12, J13	82MCMX	82MCMX-50-0-1	SUHER
18	1	L1	BLM11A121S	BLM11A121S	MURATA
19	2	L23, L28	2.2uH	LQ621N2R2K10	MURATA
20	2	L29, L24	1uH	LQ621N1R0K10	MURATA
21	2	L30, L25	680nH	LQ621N68K10	MURATA

FIG. 49A

22	2	L26, L31	1.8uH	LQ21NR8K10	MURATA
23	2	L32, L27	390nH	LQ21NR39K10	MURATA
24	4	Q1, Q5, Q10, Q14	SD404CY	SD404CY	CALOGIC
25	4	Q2, Q4, Q12, Q13	BFM505	BFM505	PHILIPS
26	4	Q3, Q7, Q11, Q16	SD213	SD213	CALOGIC
27	2	Q17, Q8	BFR520	BFR520	PHILIPS
28	4	R19, R20, R21, R83	0	ERJ3G5Y0R00	PANASONIC
29	8	R23, R26, R34, R45, R52, R57, R63, R74	33K	ERJ3G5YJ333	PANASONIC
30	4	R24, R27, R53, R58	475	ERJ3EKF4750	PANASONIC
31	6	R25, R28, R47, R54, R59, R76	402	ERJ3EKF4020	PANASONIC
32	4	R29, R30, R55, R56	221	ERJ3EKF2210	PANASONIC
33	2	R32, R61	200	ERJ3G5YJ201	PANASONIC
34	2	R33, R62	33.2K	ERJ3G5YJ333	PANASONIC
35	4	R35, R46, R64, R75	68.1	ERJ3EKF68R1	PANASONIC
36	2	R36, R65	200	ERJ3EKF2000	PANASONIC
37	6	R37, R44, R66, R73, R171, R173	49.9	ERJ3EKF49R9	PANASONIC
38	6	R40, R68, R78, R79, R80, R89	1K	ERJ3EKF1001	PANASONIC
39	2	R42, R71	62	ERJEGSYJ620	PANASONIC
40	2	R43, R72	162	ERJ3EKF1620	PANASONIC
41	2	R77, R48	DNP	ERJ3G5YJ330	PANASONIC
42	4	R81, R82, R85, R87	2K	ERJ3EKF2001	PANASONIC
43	1	R84	909	ERJ3EKF9090	PANASONIC
44	1	R88	15K	ERJ3EJF1502	PANASONIC
45	1	R90	10K	ERJ3EKF1002	PANASONIC
46	2	R91, R92	100	ERJ3EKF1000	PANASONIC
47	6	R164, R165, R166, R167, R168, R169	TBD		PANASONIC
48	2	R170, R172	OPEN		PANASONIC

FIG. 49B

49	6	TP1, TP2, TP3, TP4, TP5, TP6	TP-105-01-00		
50	2	U42, U6	NC7S04M5	NC7S04M5	NATIONAL SEMICONDUCTOR
51	1	U7	AD8052AR	AD8052AR	ANALOG DEVICES
52	1	U8	AD1582	AD1582	ANALOG DEVICES
53	1	U9	AD605AR	AD605AR	ANALOG DEVICES
54	1	U43	TK11235AMTL	TK11235BM	TOKO
55	1		BOARD	8500.541.003.V13.01	

FIG. 49C

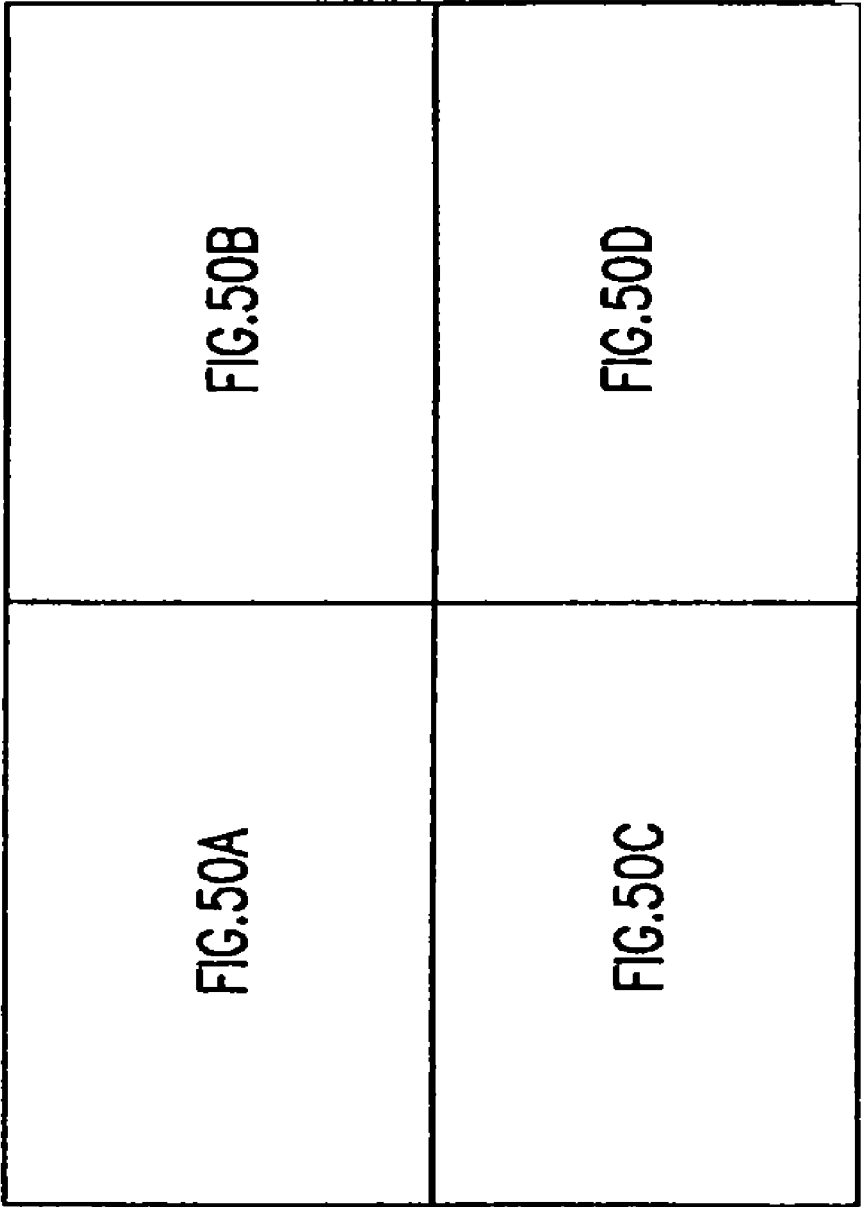
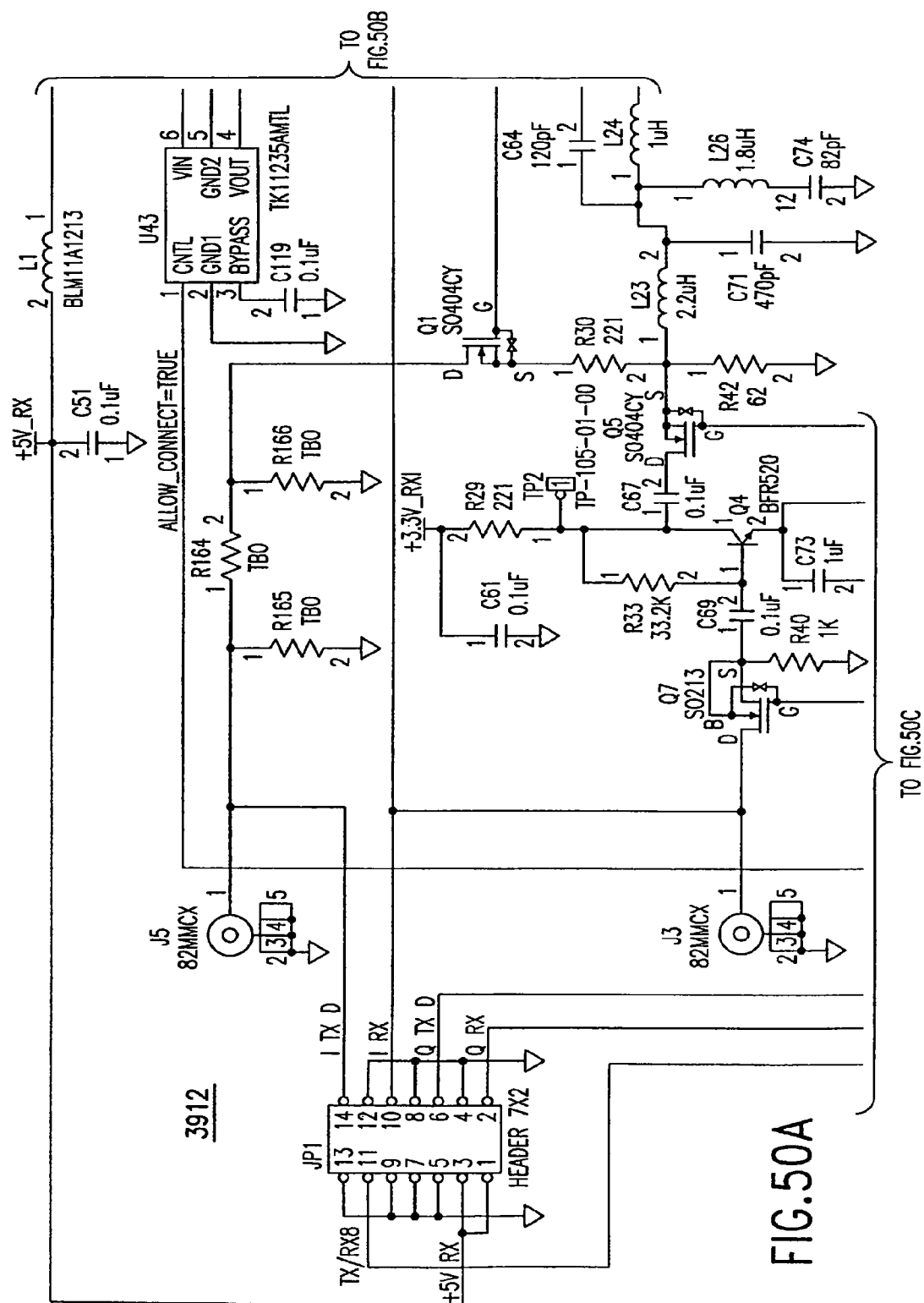
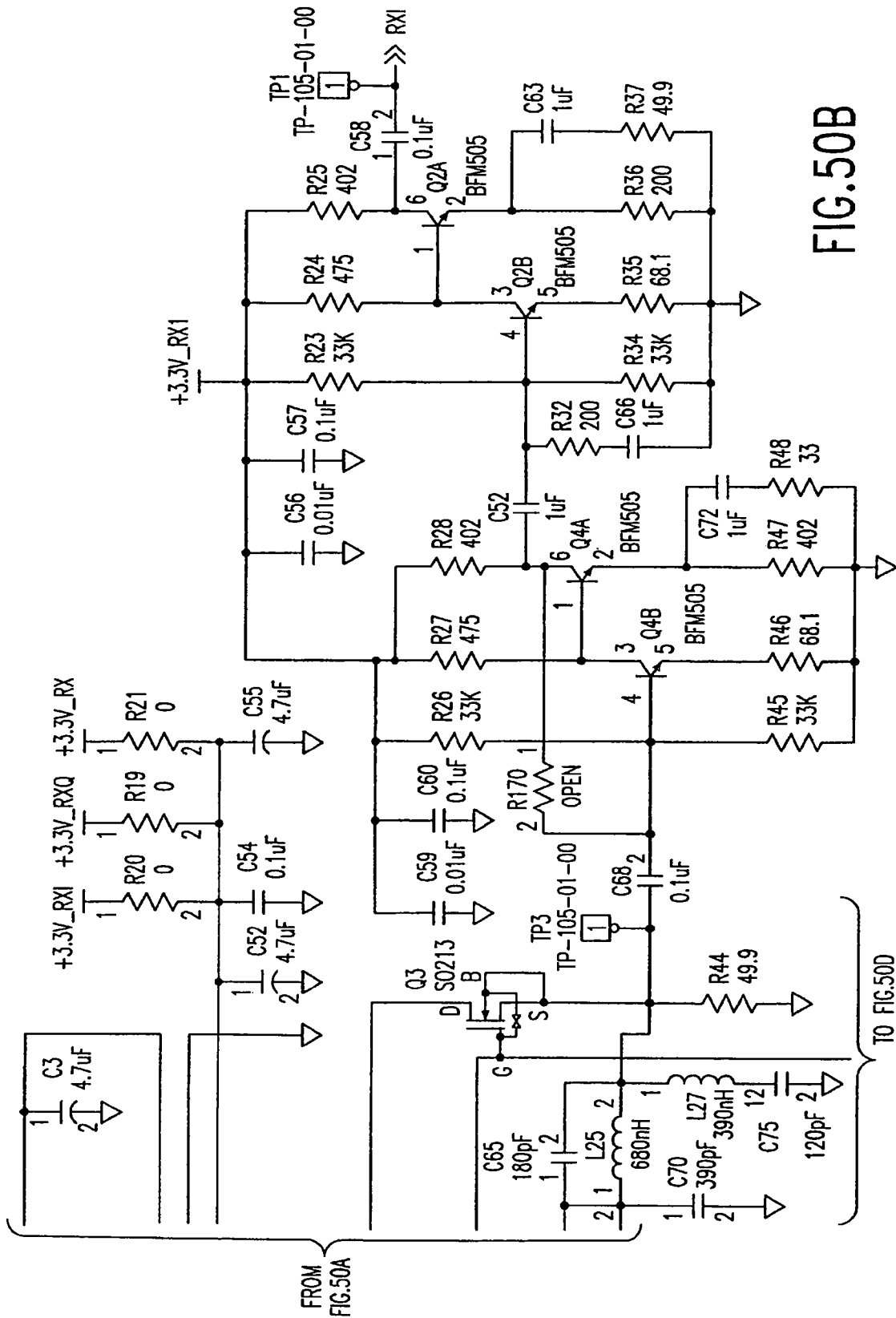
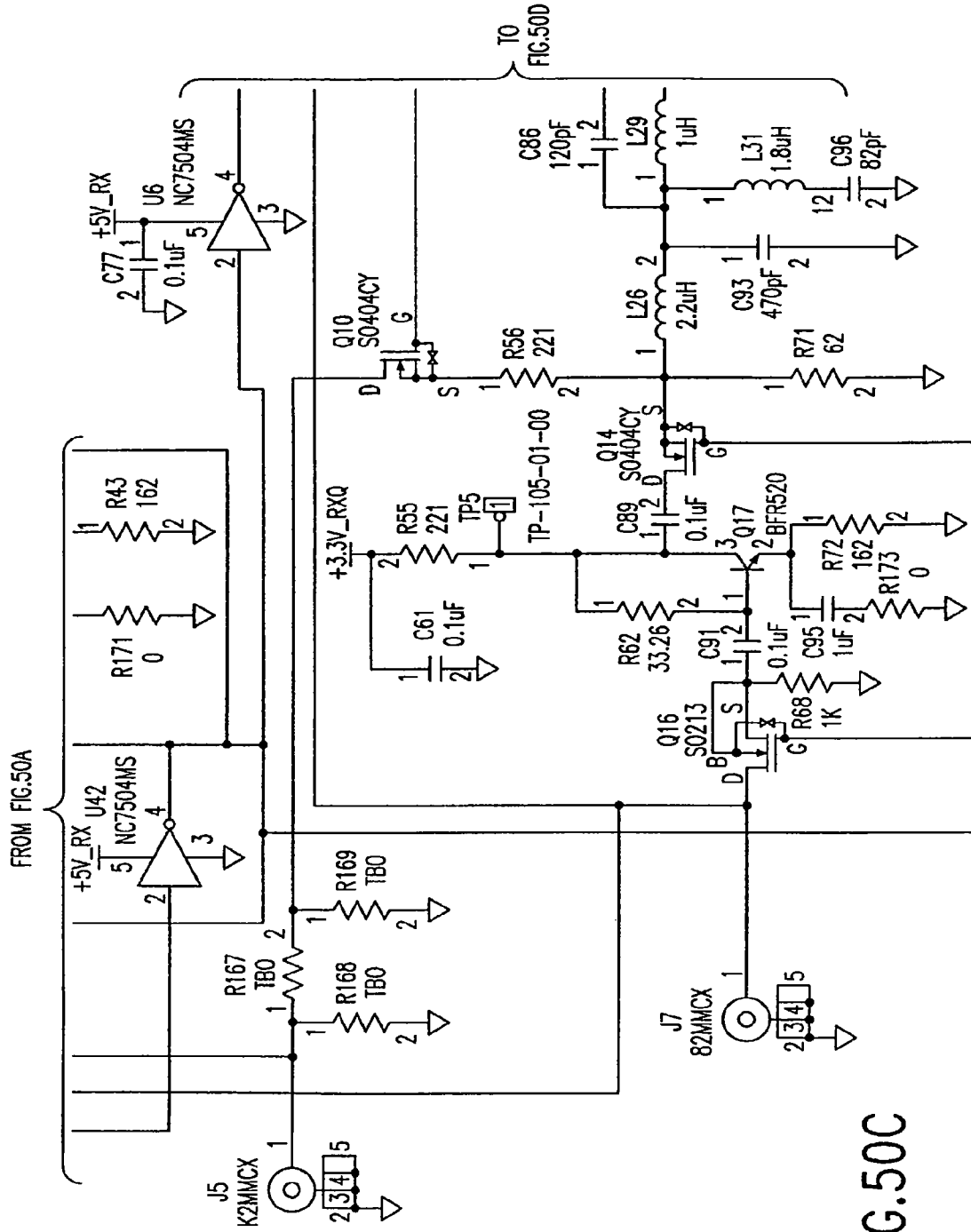


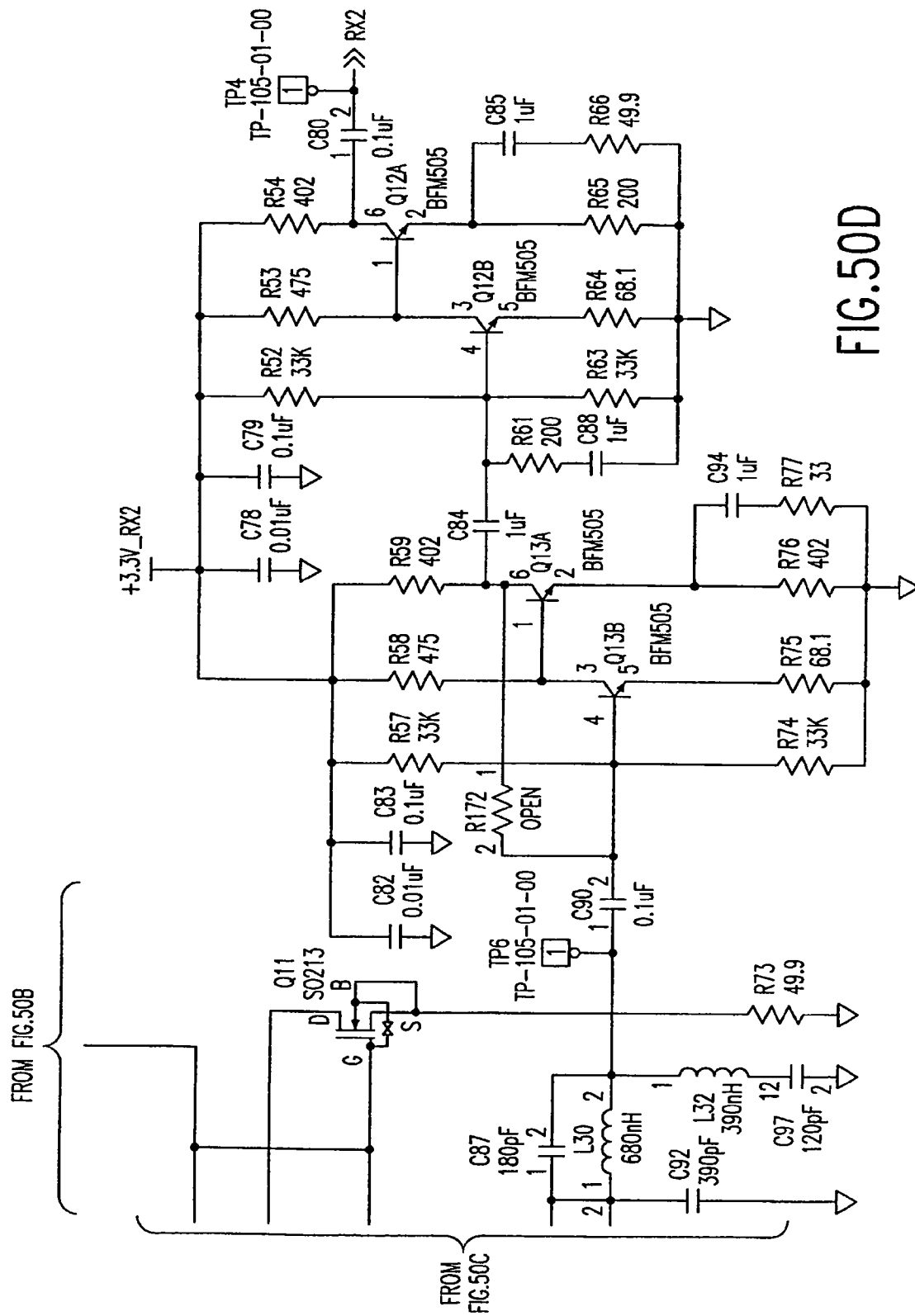
FIG. 50











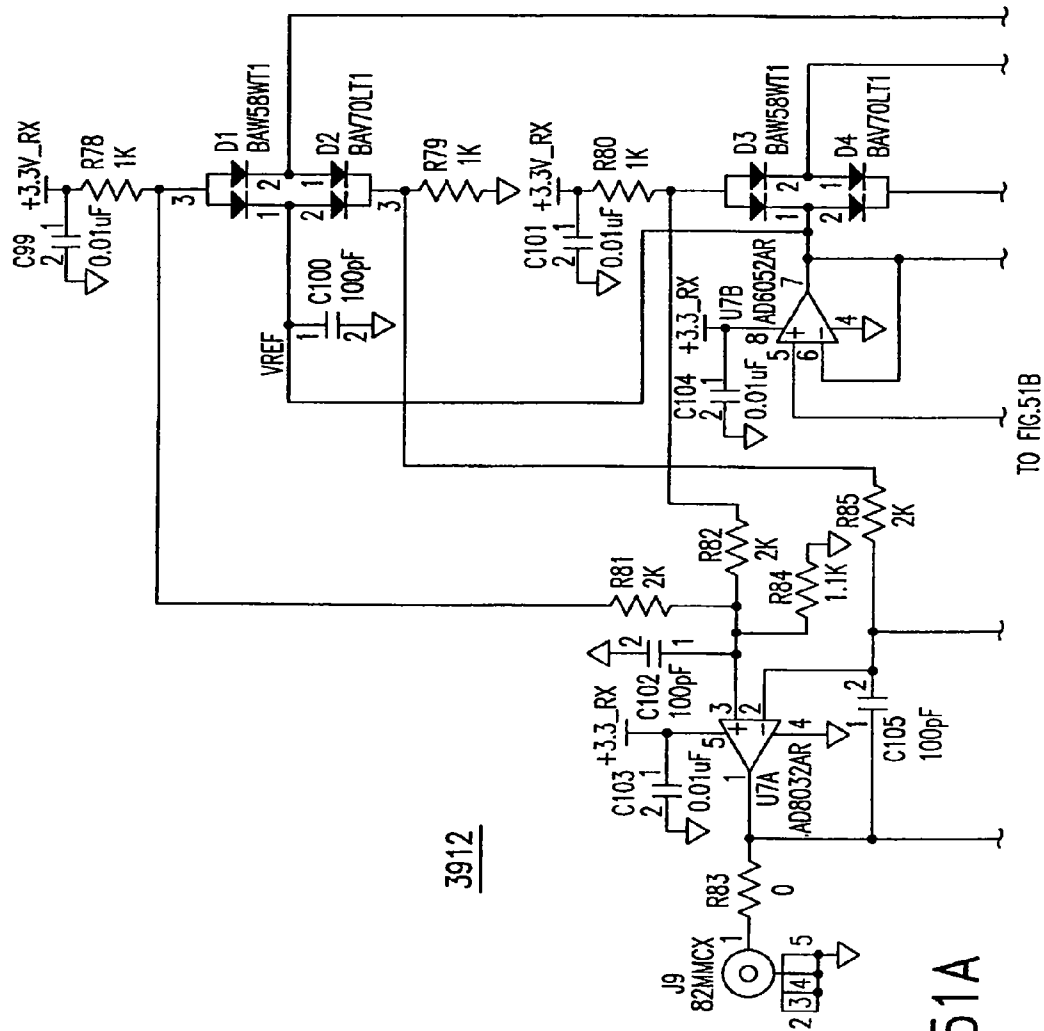


FIG. 51A

3912

TO FIG. 51B

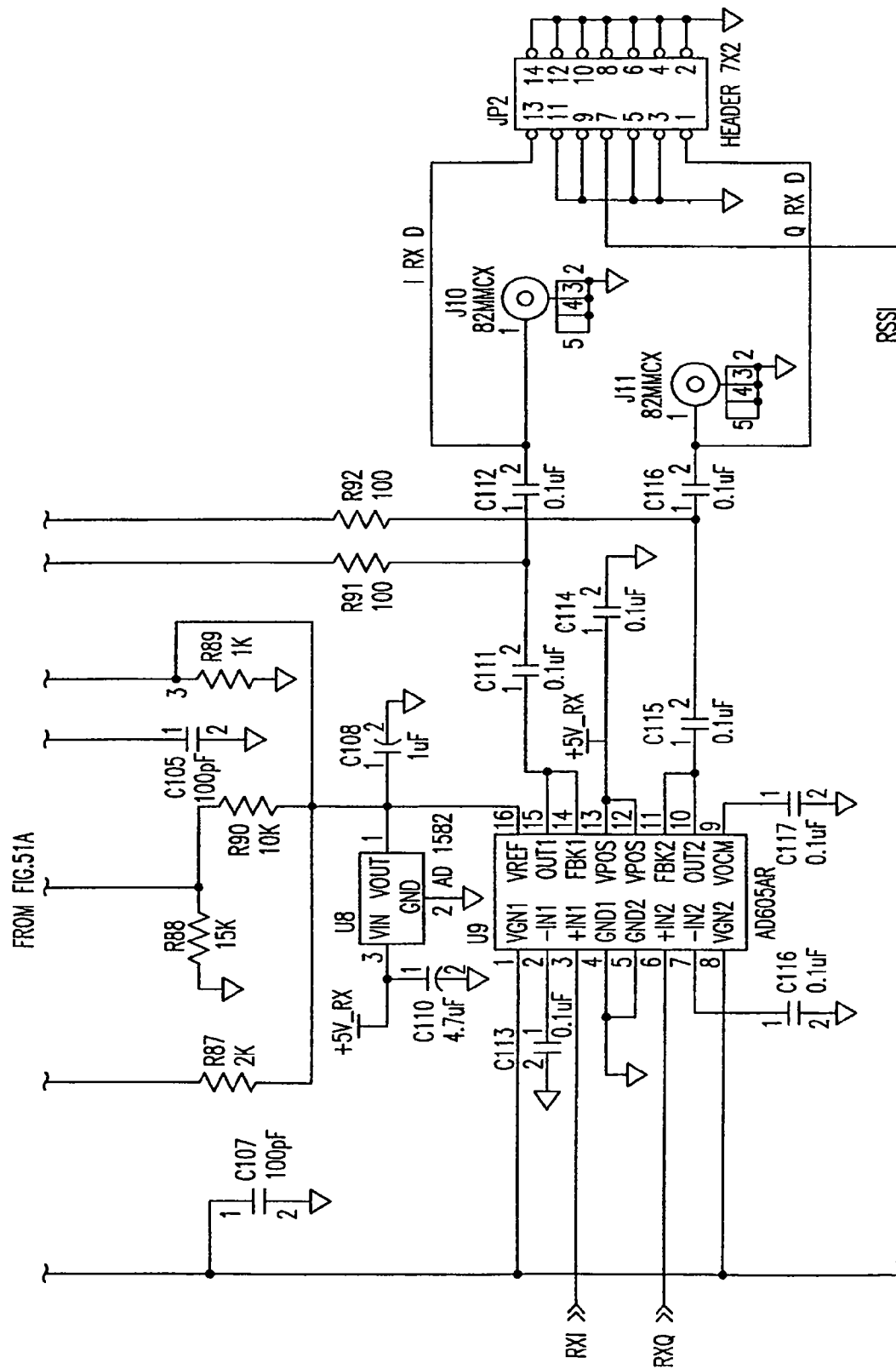


FIG. 51B

ITEM	QTY	REFERENCE	PART	PART NUMBER	MANUFACTURER
1	3	C3, C52, C55	4.7uF	T491A475K006AS	KEMET
2	26	C51, C54, C57, C58, C60, C61, C67, C68, C69, C77, C79, C80, C81, C83, C89, C90, C91, C111, C112, C113, C114, C115, C116, C117, C118, C119	0.1uF	GRM39Y5V104Z016	MURATA
3	8	C56, C59, C78, C82, C99, C101, C103, C104	0.01uF	GRM39X7R103K050	MURATA
4	10	C62, C63, C66, C72, C73, C84, C85, C88, C94, C95	1uF	GRM40Y5V105Z016	MURATA
5	4	C64, C75, C86, C97	120pF	GRM39COG121J050	MURATA
6	2	C87, C65	180pF	GRM39COG181J050	MURATA
7	2	C70, C92	390pF	GRM39COG391J050	MURATA
8	2	C71, C93	470pF	GRM39COG471J050	MURATA
9	2	C96, C74	82pF	GRM39COG820J050	MURATA
10	5	C100, C102, C105, C106, C107	100pF	GRM39COG101K050	MURATA
11	1	C108	1uF		
12	1	C110	4.7uF		
13	2	D3, D1	BAW56WT1	BAW56WT1	MOTOROLA
14	2	D4, D2	BAV70LT1	BAV70LT1	MOTOROLA
15	2	JP2, JP1	HEADER 7X2		
16	6	J1, J3, J5, J7, J10, J11	82MCMX	142-0701-231	JOHNSON
17	1	J9	82MCMX	82MCMX-50-0-1	SUHRER
18	1	L1	BLM11A121S	BLM11A121S	MURATA
19	2	L28, L23	2.2uH	LQG21N2R2K10	MURATA
20	2	L24, L29	1uH	LQG21N1R0K10	MURATA
21	2	L30, L25	680mH	LQG21NR68K10	MURATA
22	2	L26, L31	1.8uH	LQG21N1R8K10	MURATA

FIG. 52A

23	2	L27, L32	390nH	LOG21NR39K10	MURATA
24	4	Q1, Q5, Q10, Q14	SD404CY	SD404CY	CALOGIC
25	4	Q2, Q4, Q12, Q13	BFW505	BFW505	PHILIPS
26	4	Q3, Q7, Q11, Q16	SD213	SD213	CALOGIC
27	2	Q17, Q8	BFR520	BFR505	PHILIPS
28	5	R19, R20, R21, R171, R173	0		
29	8	R23, R26, R34, R45, R52, R57, R63, R74	33K	ERJ3GSY333	PANASONIC
30	4	R24, R27, R53, R58	475	ERJ3EKF4750	PANASONIC
31	6	R25, R28, R47, R54, R59, R76	402	ERJ3EKF4020	PANASONIC
32	4	R29, R30, R55, R56	221	ERF3EKF2210	PANASONIC
33	2	R32, R61	200	ERJ3GSYJ201	PANASONIC
34	2	R33, R62	33.2K	ERJ3GSYJ333	PANASONIC
35	4	R35, R46, R64, R75	68.1	ERJ3EKF68R1	PANASONIC
36	2	R36, R65	200	ERJ3EKF2000	PANASONIC
37	2	R66, R37	49.9	ERJ3EKF49R9	PANASONIC
38	6	R40, R68, R78, R79, R80, R89	1K	ERJ3EKF1001	PANASONIC
39	2	R42, R71	62	ERJ3GSYJ620	PANASONIC
40	2	R43, R72	162	ERJ3EKF6810	PANASONIC
41	2	R44, R73	49.9	ERJ3EKF1001	PANASONIC
42	2	R77, R48	33	ERJ3GSYJ330	PANASONIC
43	4	R81, R82, R85, R87	2K	ERJ3EKF2001	PANASONIC
44	1	R83	0	ERJGSY0R00	PANASONIC
45	1	R84	1.1K	ERJ3EKF2001	PANASONIC
46	1	R88	15K	ERJ3EKF1502	PANASONIC
47	1	R90	10K	ERJ3EKF1002	PANASONIC
48	2	R91, R92	100	ERJ3EKF1000	PANASONIC
49	6	R164, R165, R166, R167, R168, R169	TBD		
50	2	R170, R172	OPEN		

FIG. 52B

51	0	TP1, TP2, TP3, TP4, TP5, TP6	TP-105-01-00		
52	2	U42, U6	NC7S04M5		NATIONAL SEMICONDUCTOR
53	1	U7	AD8032AR	AD8032AR	ANALOG DEVICES
54	1	U8	AD1582	AD1582	ANALOG DEVICES
55	1	U9	AD605AR	AD605AR	ANALOG DEVICES
56	1	U43	TK11235AMTL	TK11235AMTL	TOKO

FIG.52B-1

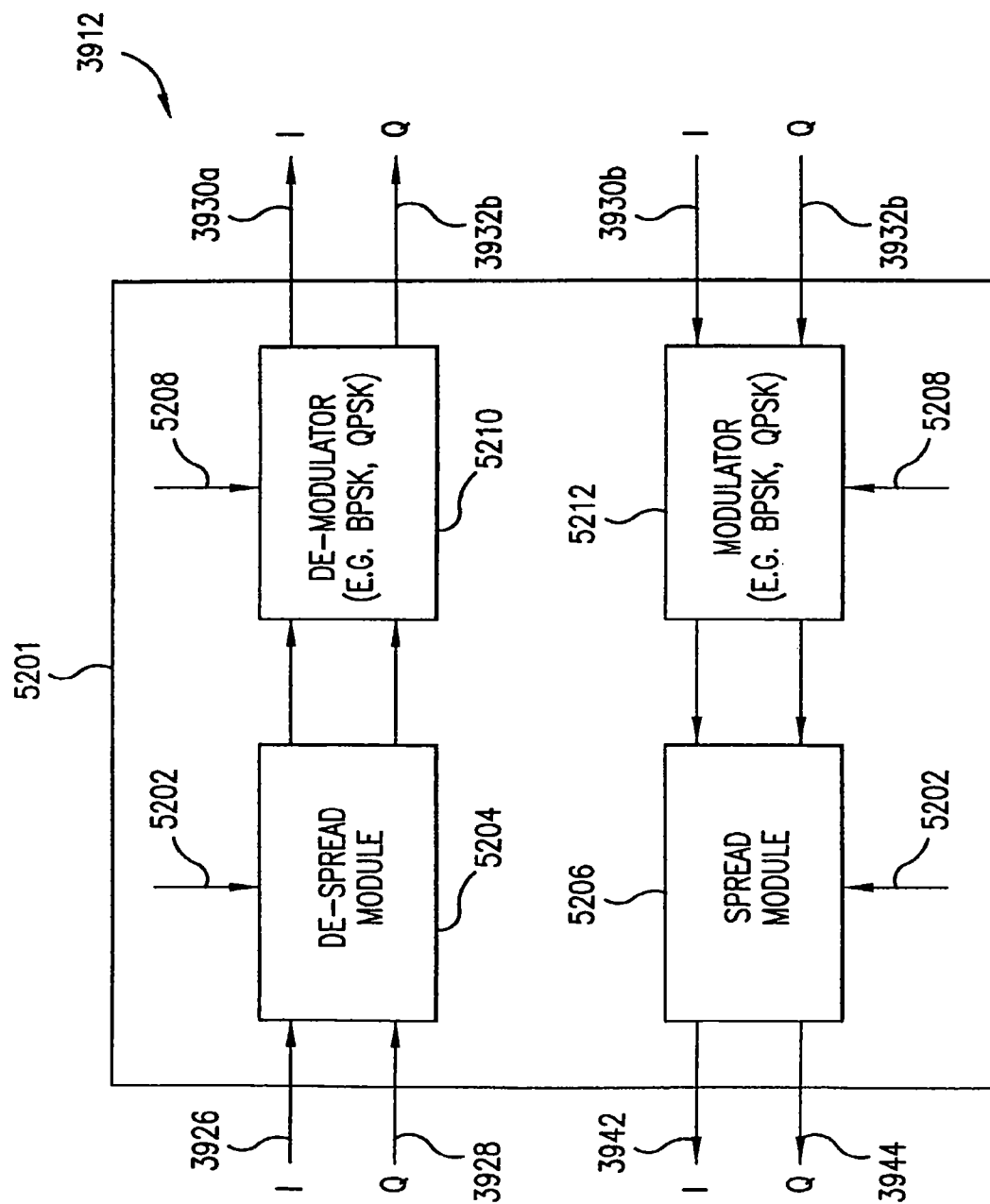
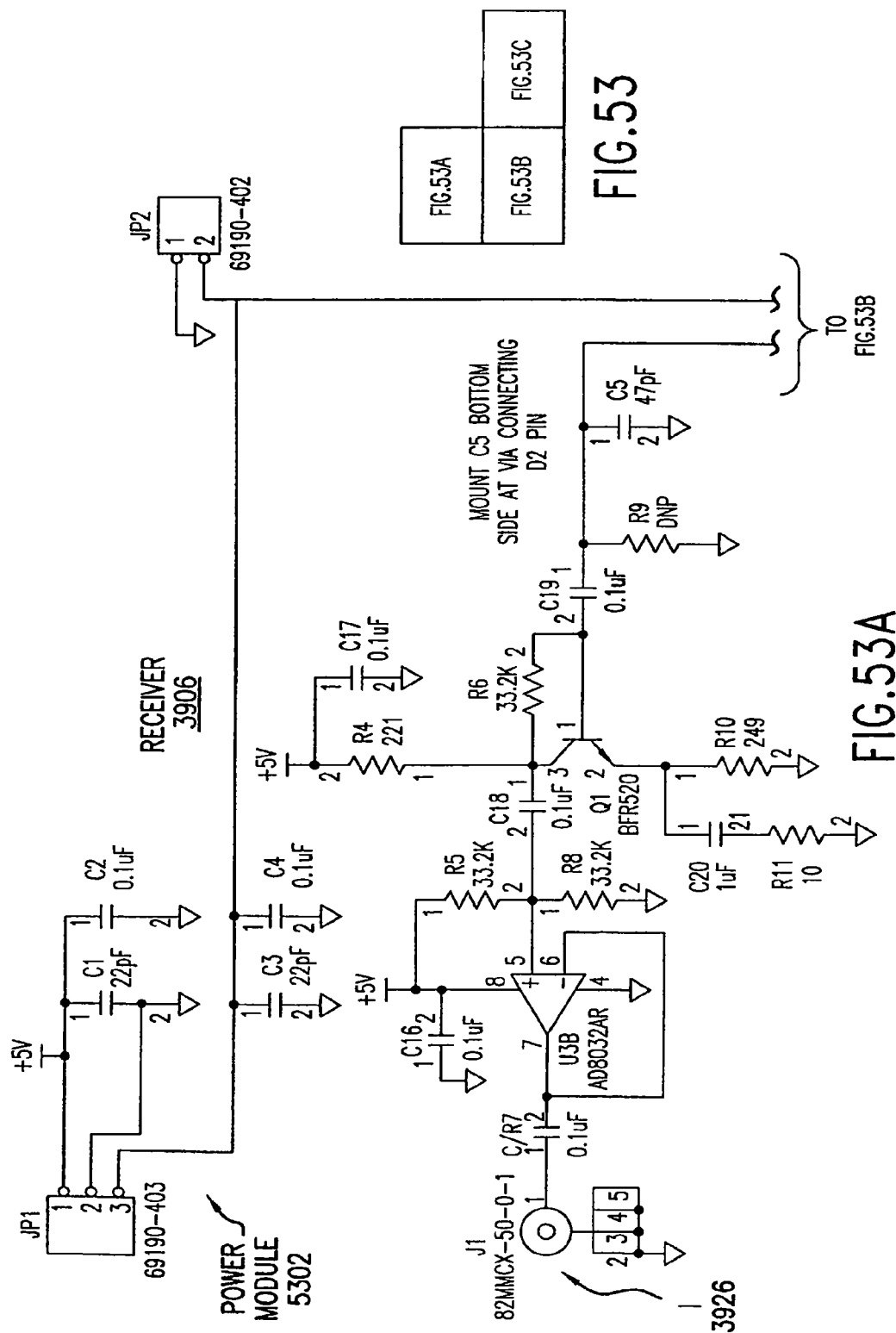
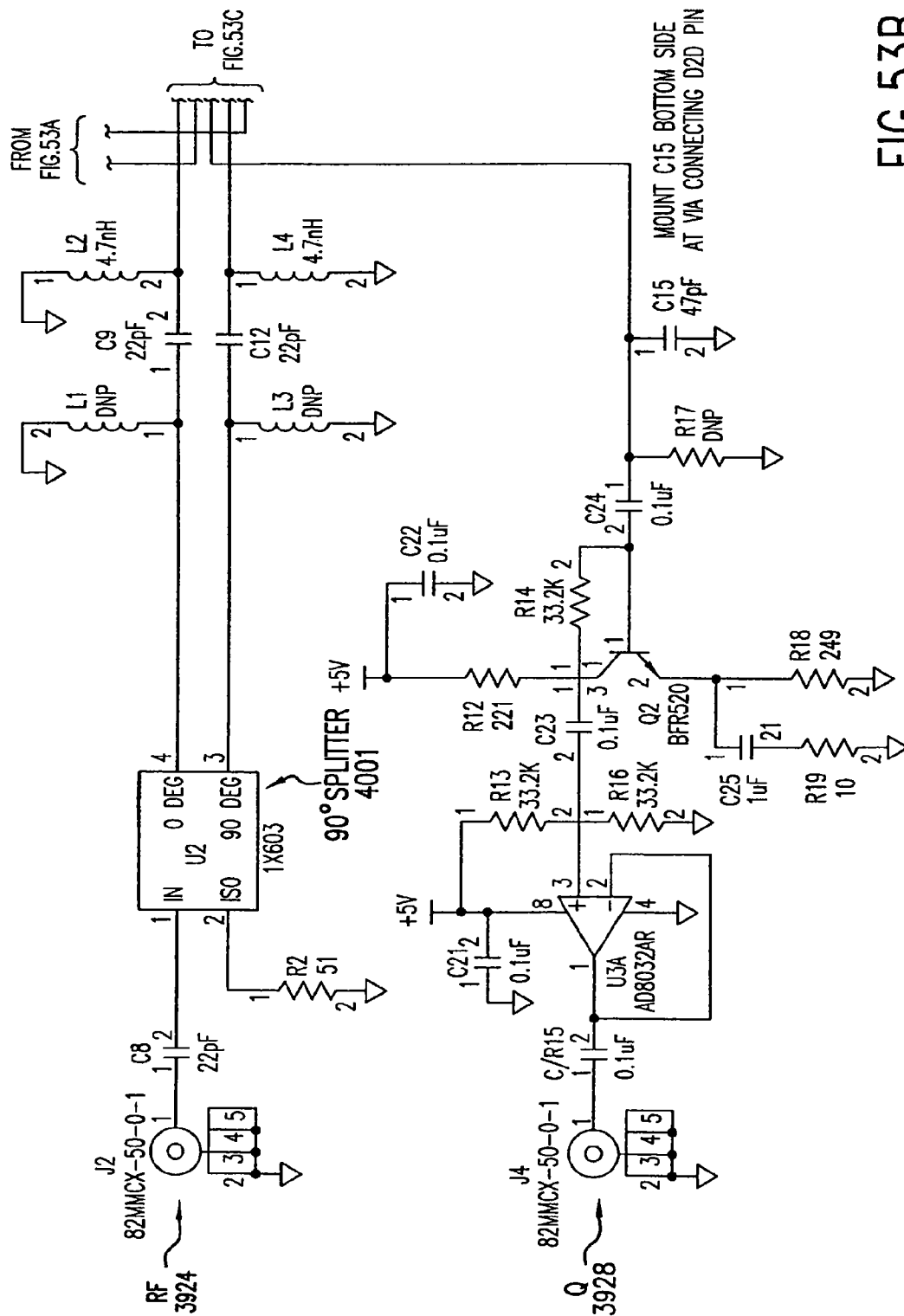


FIG. 52C







**FIG. 53B**

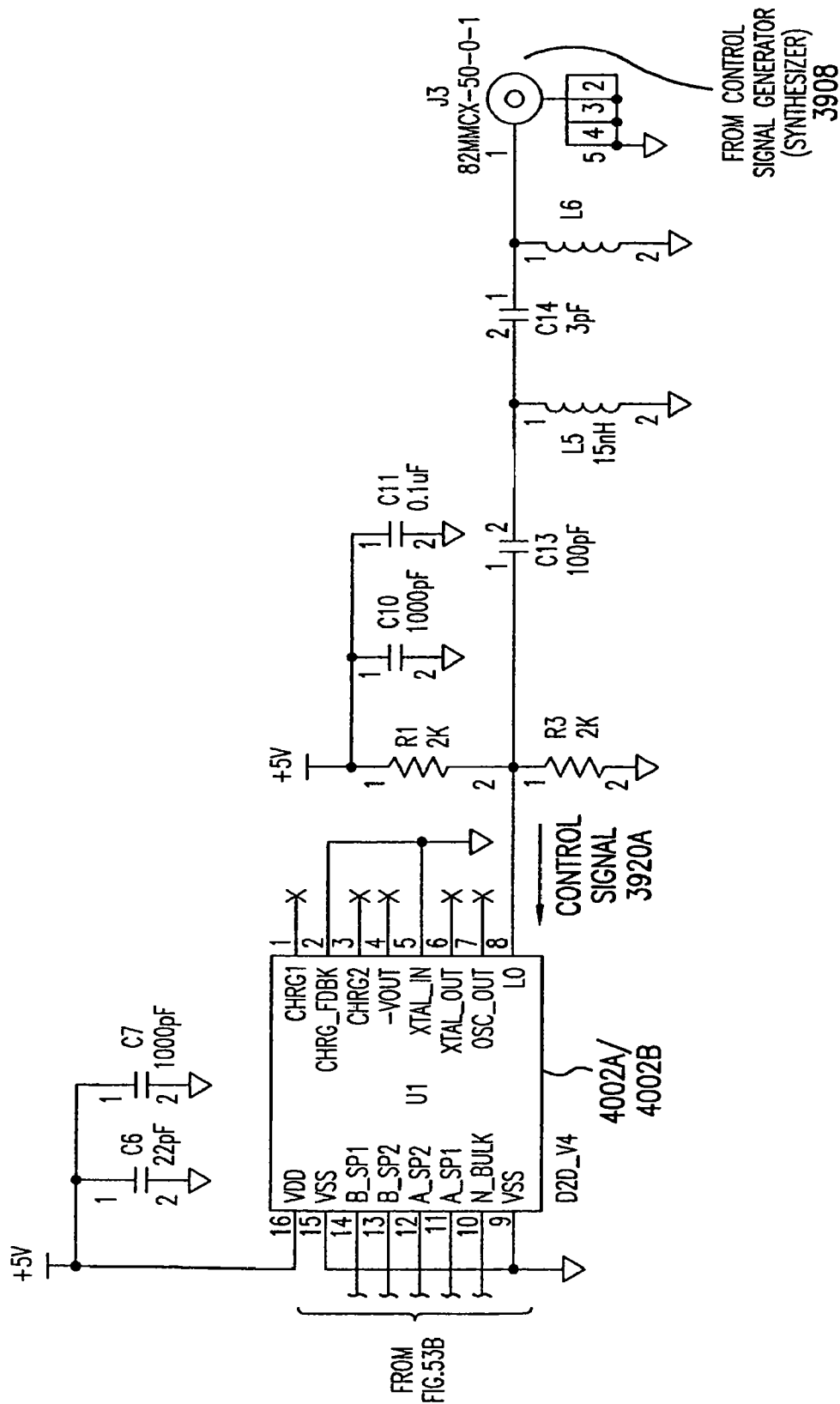


FIG. 53C

ITEM	QTY	REFERENCE	PART	PART NUMBER	MANUFACTURER
1	10	C/R7,C/R15,C16,C17,C18 C19,C21,C22,C23,C24	0.1uF	GRM39Y5V104Z016	MURATA
2	6	C1,C3,C6,C8,C9,C12	22pF	GRM39CCG220J050	MURATA
3	3	C2,C4,C11	0.1uF	GRM39X7R104K016	MURATA
4	2	C5,C15	47pF	GRM39CCG470J050	MURATA
5	2	C10,C7	1000pF	GRM39X7R102K050	MURATA
6	1	C13	100pF	GRM39X7R101J050	MURATA
7	1	C14	3pF	GRM40CCG030B50V	MURATA
8	2	C20,C25	1uF	GRM40Y5V105Z016	MURATA
9	1	JP1	69190-403	69190-403	BERG
10	1	JP2	69190-402	69190-402	BERG
11	4	J1,J2,J3,J4	82MCMX-50-0-1	82MCMX-50-0-1	SUHRER
12	2	L3,L1	DNP	L	TOKO
13	2	L4,L2	4.7nH	LL1608-F4N7K	TOKO
14	1	L5	15nH	LL2012FH15NJ	TOKO
15	1	L6	DNP	DNP	TOKO
16	2	Q1,Q2	BFR520	BFR520	PHILIPS
17	2	R1,R3	2K	ERJ3G5YJ202	PANASONIC
18	1	R2	51	ERJ3G5YJ510	PANASONIC
19	2	R4,R12	221	ERJ3EKF2210	PANASONIC
20	6	R5,R6,R8,R13,R14,R16	33.2K	ERJ3EKF3322	PANASONIC
21	2	R9,R17	DNP	ERJ3EKF1001	PANASONIC
22	2	R10,R18	249	ERJ3EKF2490	PANASONIC
23	2	R11,R19	10	ERJ3G5YJ100	PANASONIC
24	1	U1	D2D_V4	D2D_V4	PARKER VISION
25	1	U2	1X603	1X603	ANAREN
26	1	U3	AD8032AR	AD8032AR	ANALOG DEVICES
27	1		BOARD	SB500.641.001 V03.00	

FIG. 54

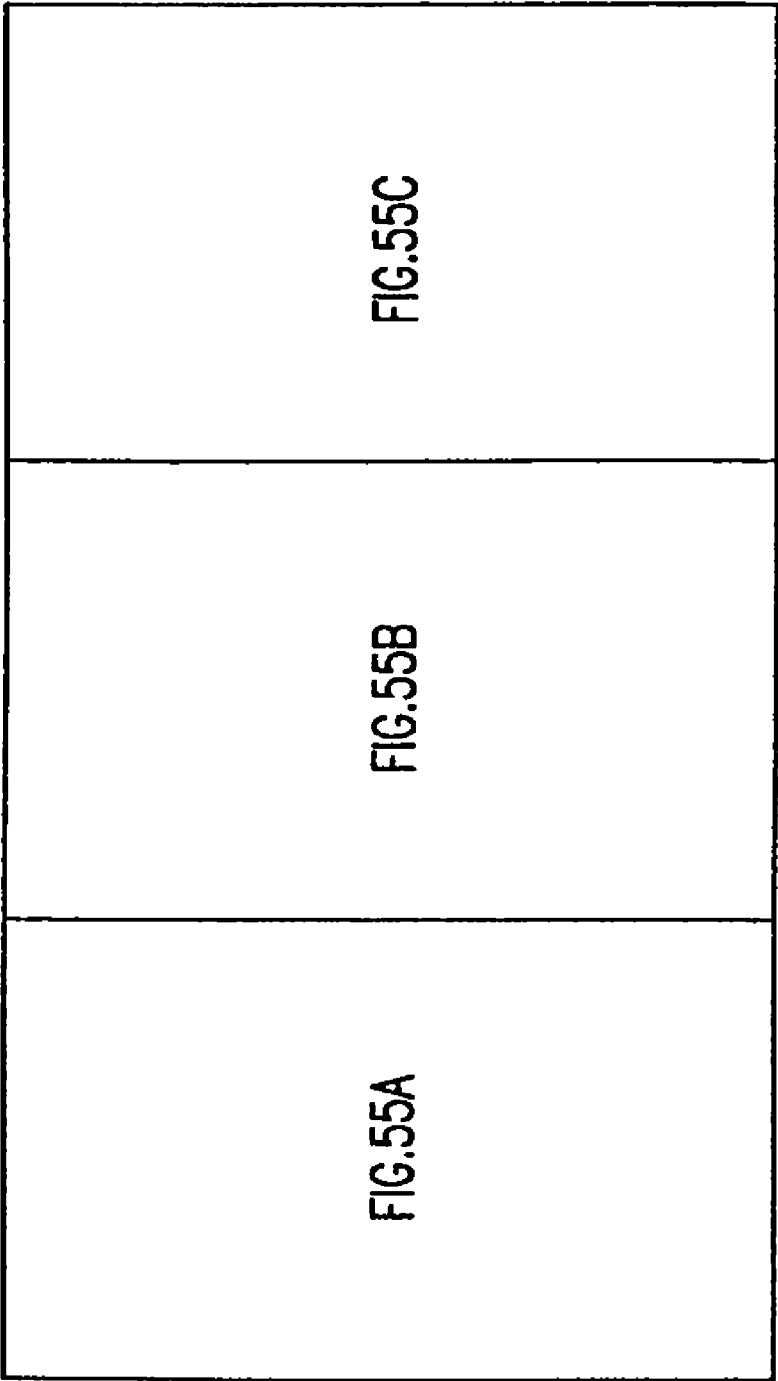


FIG. 55

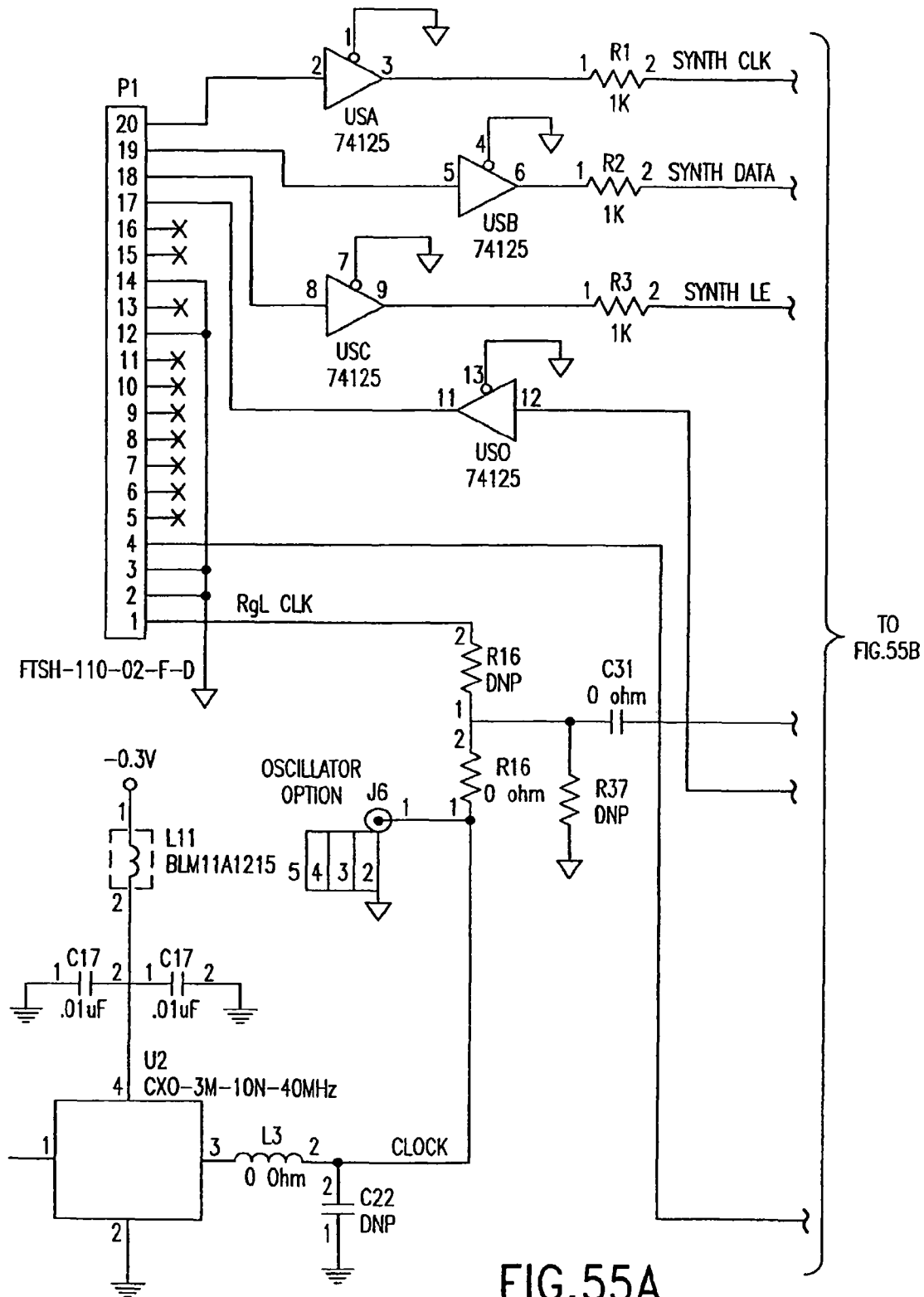


FIG. 55A

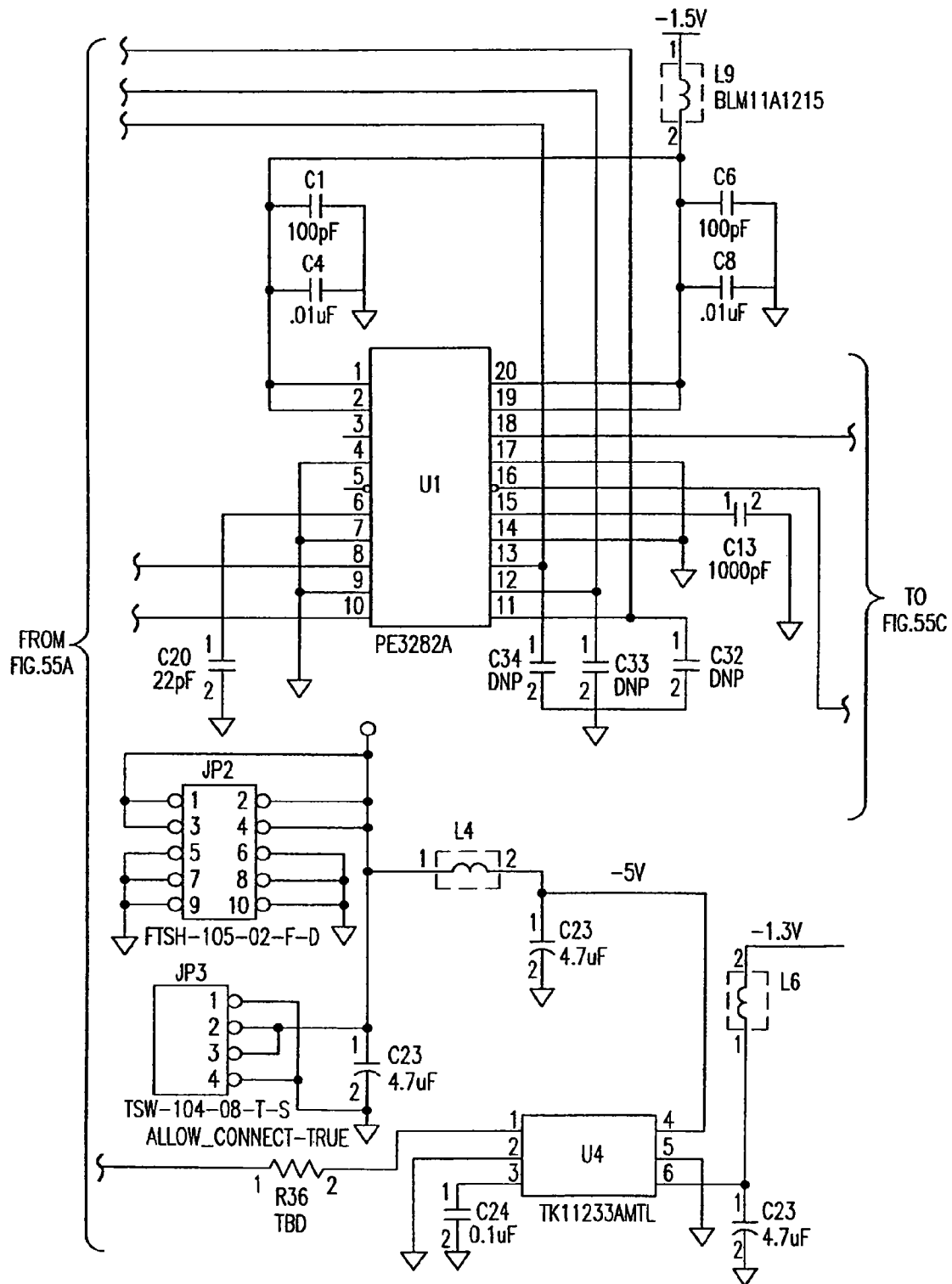


FIG. 55B

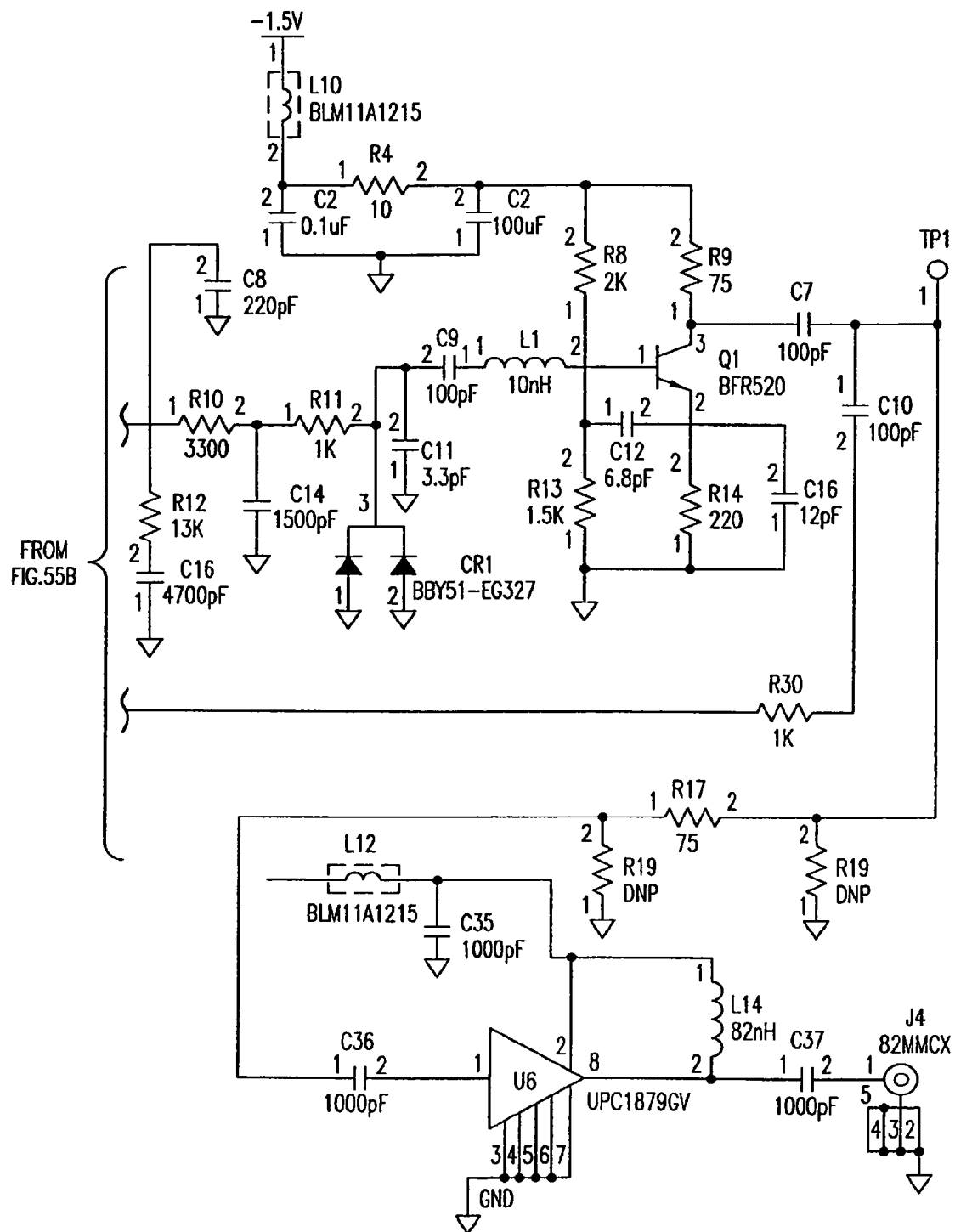


FIG.55C

ITEM QTY	REFERENCE	PART	DESCRIPTION	PART NUMBER	MANUFACT.
1 1	CR1	BBY51-E6327	DIODE, VARACTOR	BBY51-E6327	SIEMENS
2 6	C1, C3, C5, C7, C9, C10	100pF	CAPACITOR, CERAMIC, 100pF, 10%, C0G, 0603	GRM39CCG101K050	MURATA
3 2	C29, C2	0.1uF	CAPACITOR, CERAMIC, .1uF, 10%, X7R, 0603	GRM39X7R104K016AD	MURATA
4 3	C4, C8, C17	.01uF	CAPACITOR, CERAMIC, .01uF, 10%, X7R, 0603	GRM39X7R103K050	MURATA
5 1	C6	220pF	CAPACITOR, CERAMIC, 220pF, 5%, C0G, 0603	GRM39CCG221J025	MURATA
6 1	C11	3.3pF	CAPACITOR, CERAMIC, 3.3pF, 5%, C0G, 0603	GRM39CCG3R3B100V	MURATA
7 1	C12	6.8pF	CAPACITOR, CERAMIC, 6.8pF, +/- .25pF, C0G, 0603	GRM39CCG6R8C100V	MURATA
8 4	C13, C35, C36, C37	1000pF	CAPACITOR, CERAMIC, 1000pF, 10%, X7R, 0603	GRM39X7R102K016	MURATA
9 1	C14	1500pF	CAPACITOR, CERAMIC, 1500pF, 10%, X7R, 0603	GRM39X7R152K016	MURATA
10 1	C15	12pF	CAPACITOR, CERAMIC, 12pF, 5%, C0G, 0603	GRM39CCG120J050	MURATA
11 1	C16	4700pF	CAPACITOR, CERAMIC, 4700pF, 10%, 0603	GRM39X7R472K016	MURATA
12 2	C20, C18	22pF	CAPACITOR, CERAMIC, 22pF, 10%, C0G, 0603	GRM36CCG220K050	MURATA
13 4	C22, C32, C33, C34	DNP	CAPACITOR, CERAMIC, . . . , 0603		MURATA
14 3	C23, C24, C27	4.7uF	CAPACITOR, TANTALUM, 4.7uF, 10%, 3216	T491A475K006AS	KEMET
15 3	R16, C31, R17	0 OHM	RESISTOR, ZERO OHM, 0603	ERJ3GSYQR00	PANASONIC
16 1	JP1	FTSH-110-02-F-D	HEADER, DUAL ROW 10X2, .050X.050	FTSH-110-02-F-D	SAMTEC
17 1	JP2	FTSH-105-02-F-D	HEADER, DUAL ROW 5X2, .050X.050	FTSH-105-02-F-D	SAMTEC
18 1	JP3	TSW-104-08-T-S	HEADER, SINGLE ROW 4 PIN, .100"	TSW-104-08-T-S	BERG
19 2	J5, J6	82MMCX	RF CONNECTOR	82MMCX-50-0-1	SUHRER
20 1	L1	18nH	INDUCTOR, 18nH, 10%, 0805	0805CS-180XJBC	COILCRAFT
21 1	L3	0 OHM	ZERO OHM JUMPER	RM73Z1JT	KOA
22 6	L4, L6, L9, L10, L11, L12	BLM11A121S	FERRITE BEAD, 0603	BLM11A121S	MURATA
23 1	L14	82nH	INDUCTOR, 82nH, 10%, 0805	LL2012-F82NK	TOKO
24 1	Q1	BFR520	TRANSISTOR, NPN	BFR520	PHILIPS
25 5	R1, R2, R3, R11, R30	1K	RESISTOR, 1K, 5%, 0603	ERF3GSYJ102	PANASONIC
26 1	R4	10	RESISTOR, 10 OHM, 5%, 0603	ERJ3GSYJ1R0	PANASONIC

FIG. 56A



27	1	R8	2K	RESISTOR, 2K, 5%, 0603	ERJ36SYJ202	PANASONIC
28	1	R9	75	RESISTOR, 75 OHM, 5%, 0603	ERJ36SYJ750	PANASONIC
29	1	R10	3300	RESISTOR, 3.3K, 5%, 0603	ERJ36SYJ332	PANASONIC
30	1	R12	13K	RESISTOR, 13K, 5%, 0603	ERJ36SYJ133	PANASONIC
31	1	R13	1.5K	RESISTOR, 1.5K, 5%, 0603	ERJ36SYJ152	PANASONIC
32	1	R14	220	RESISTOR, 220 OHM, 5%, 0603	ERJ36SYJ221	PANASONIC
33	1	R15	DNP	RESISTOR, ZERO OHM, 0603	ERJ36SYOR00	PANASONIC
34	2	R18, R19	DNP	RESISTOR, 91 OHM, 5%, 0603	ERJ36SYJ910	PANASONIC
35	1	R36	TBD	RESISTOR, ZERO OHM, 0603	ERJ36SYOR00	PANASONIC
36	1	R37	DNP	RESISTOR, , , 0603		PANASONIC
37	1	TP1	TEST POINT			
38	1	U1	PE3282A	IC, SYNTHESIZER	PE3282A	PEREGRINE
39	1	U2	CXO-3M-10N-40MHz	XTAL OSC, 40MHz	CXO-3M-10N-40MHZ A/I	STATEK
40	1	U4	TK11233AMTL	VOLTAGE REGULATOR, 3.5V	TK11235BM	TOKO
41	1	U5	74125	IC, BUFFER	MC74LCX1250T	MOTOROLA
42	1	U6	UPC1678GV	IC, RF AMPLIFIER	UPC1678GV	NEC
43	1		STB500.641.008 V03.00	BOARD		

FIG. 56B

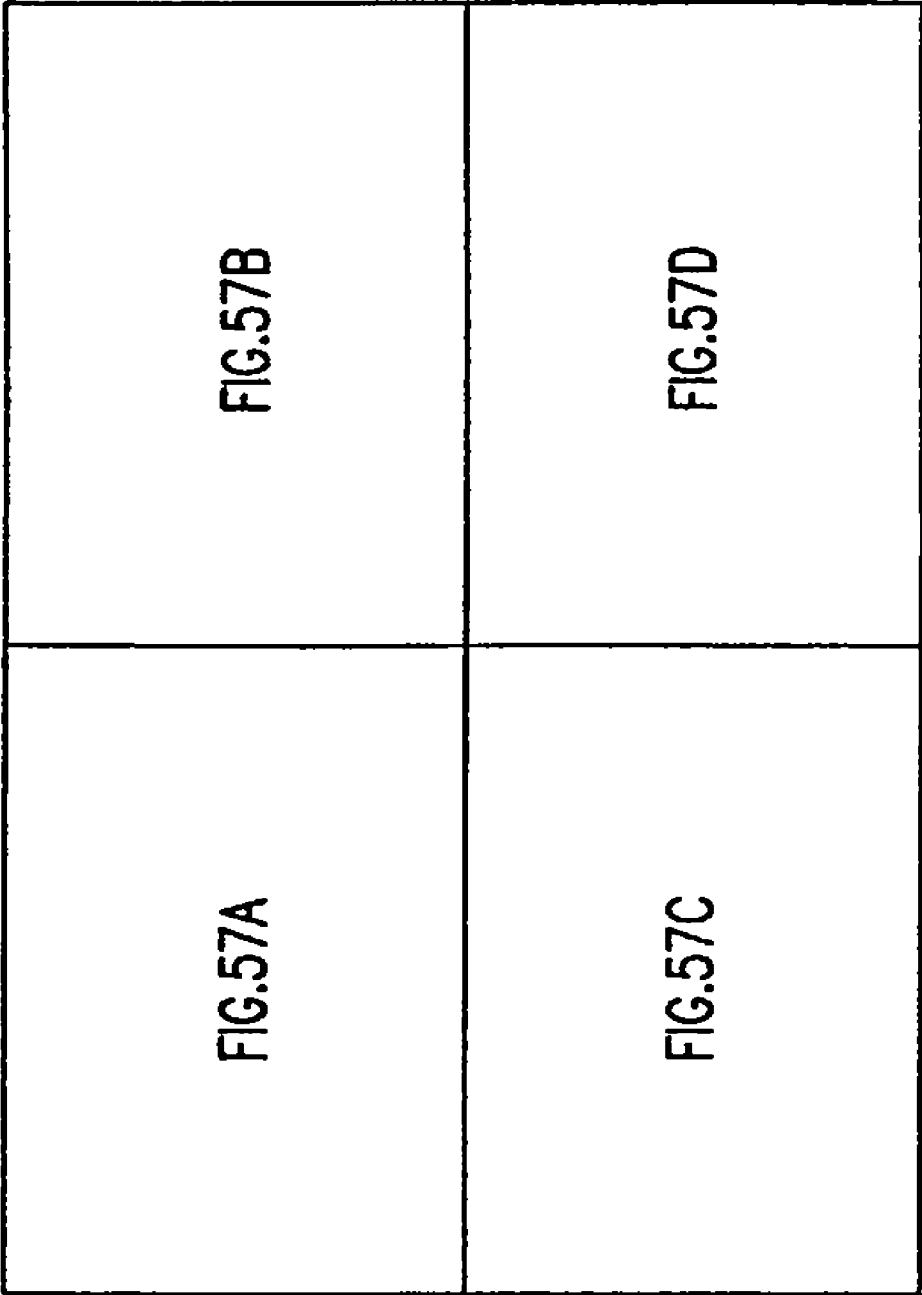
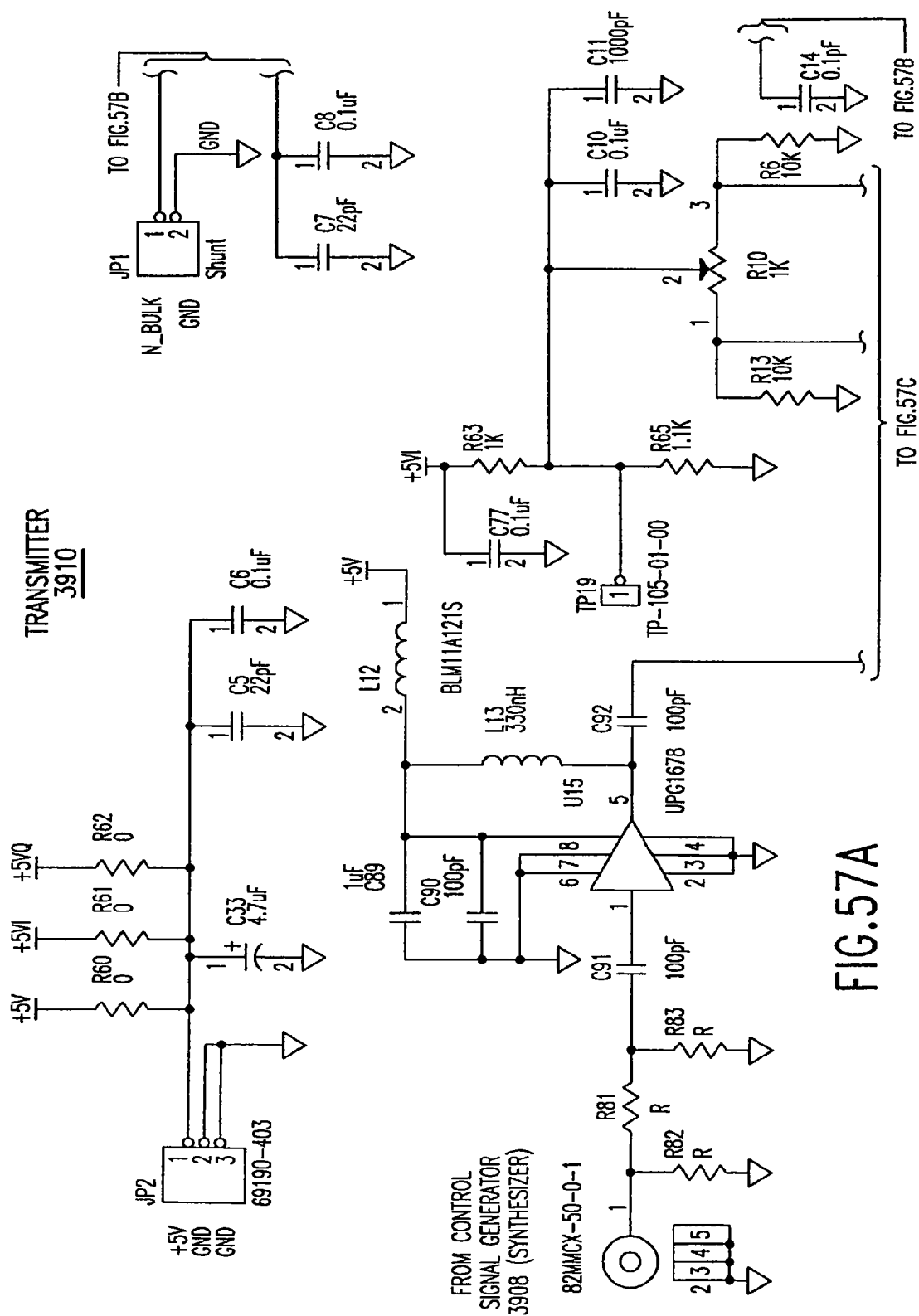
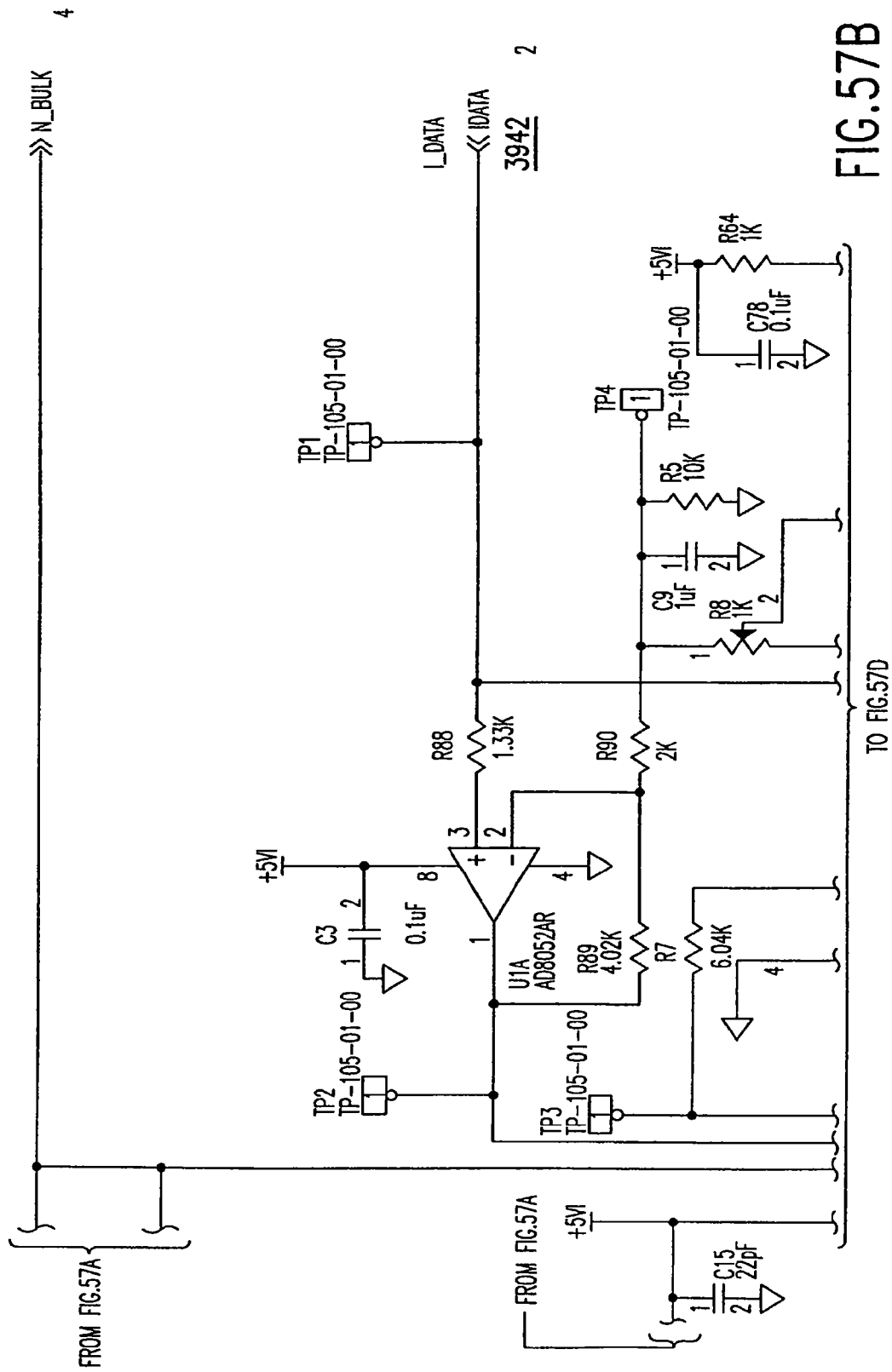


FIG.57





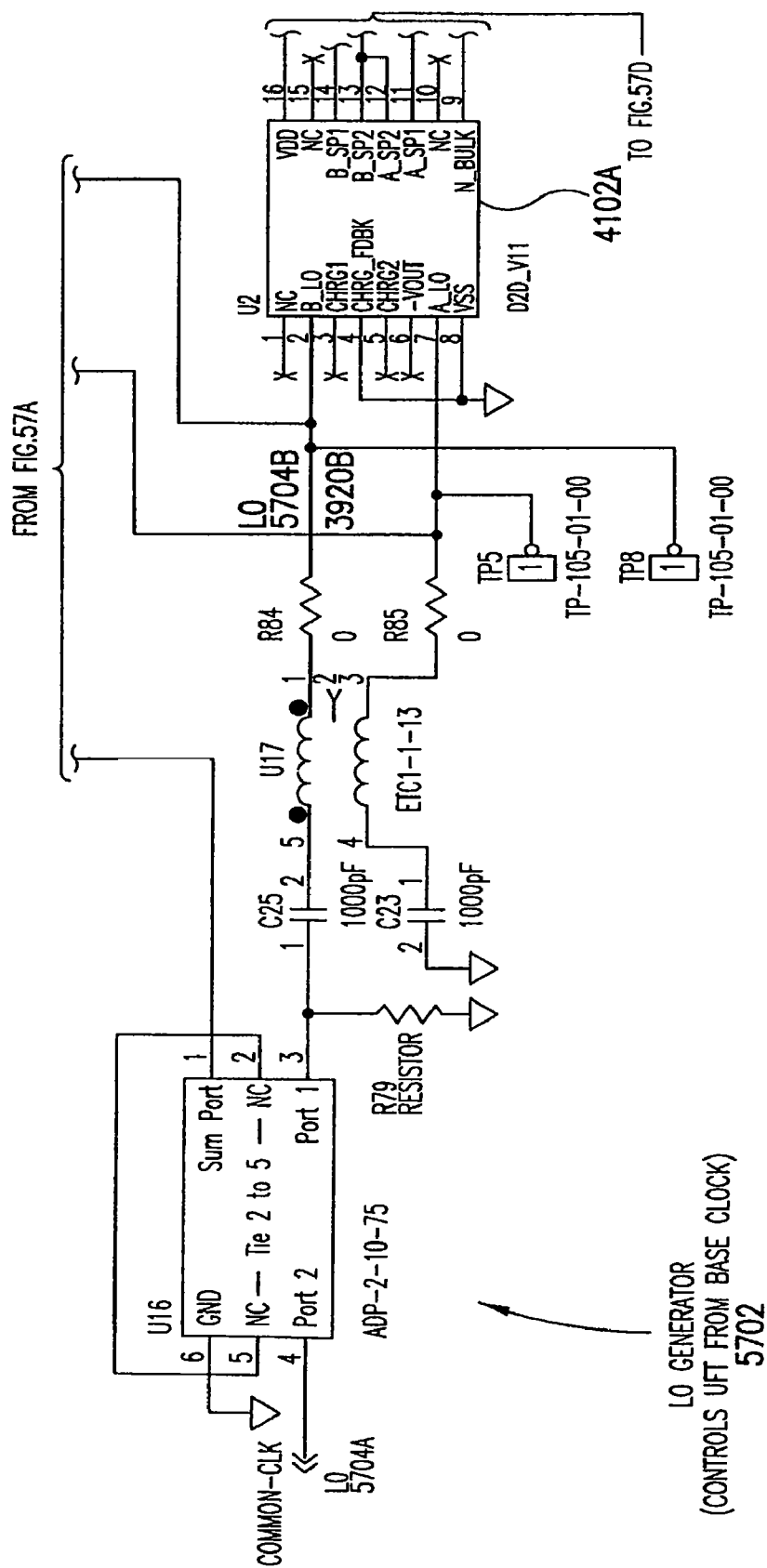
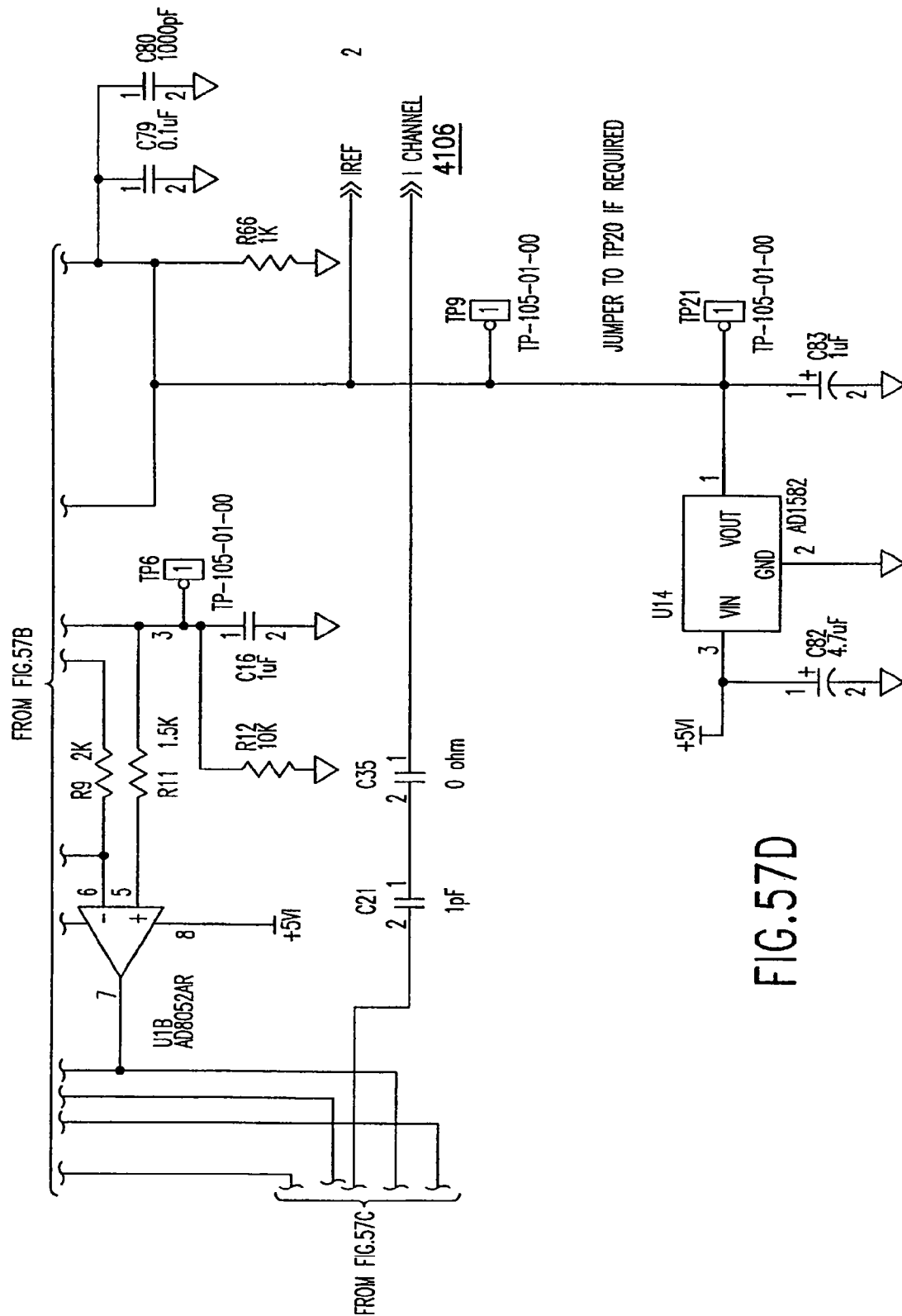


FIG. 57C



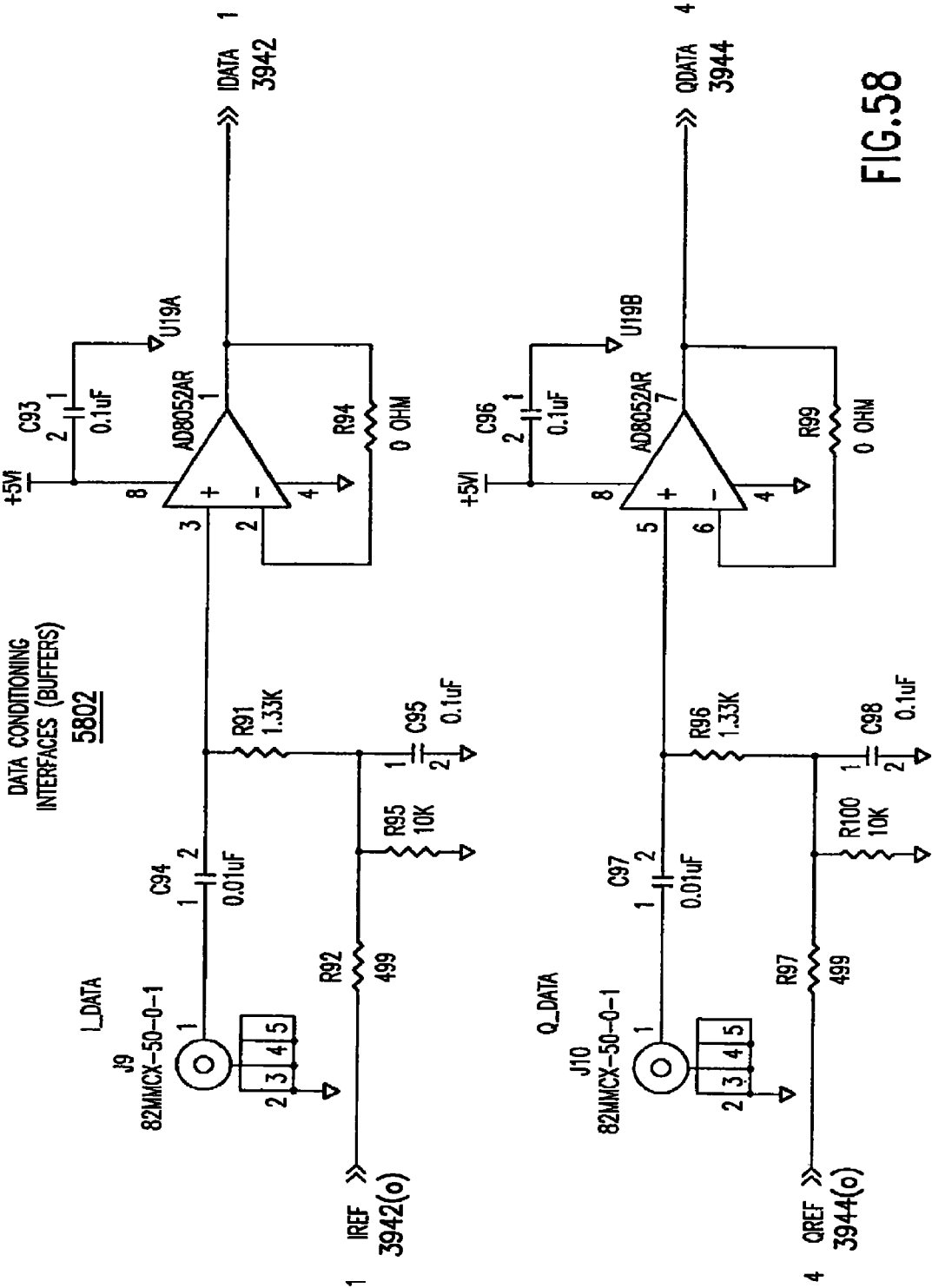


FIG.58

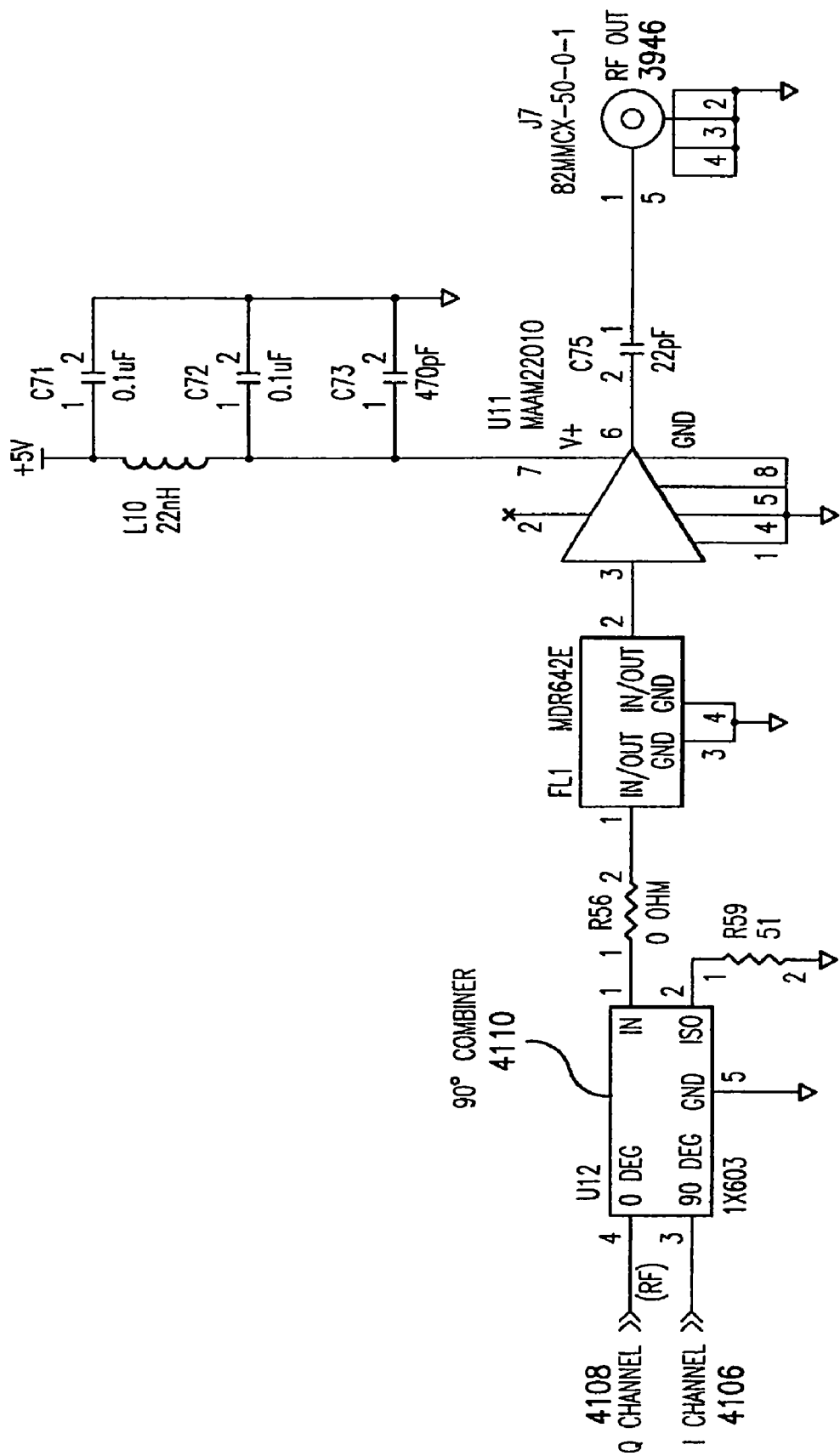


FIG.59



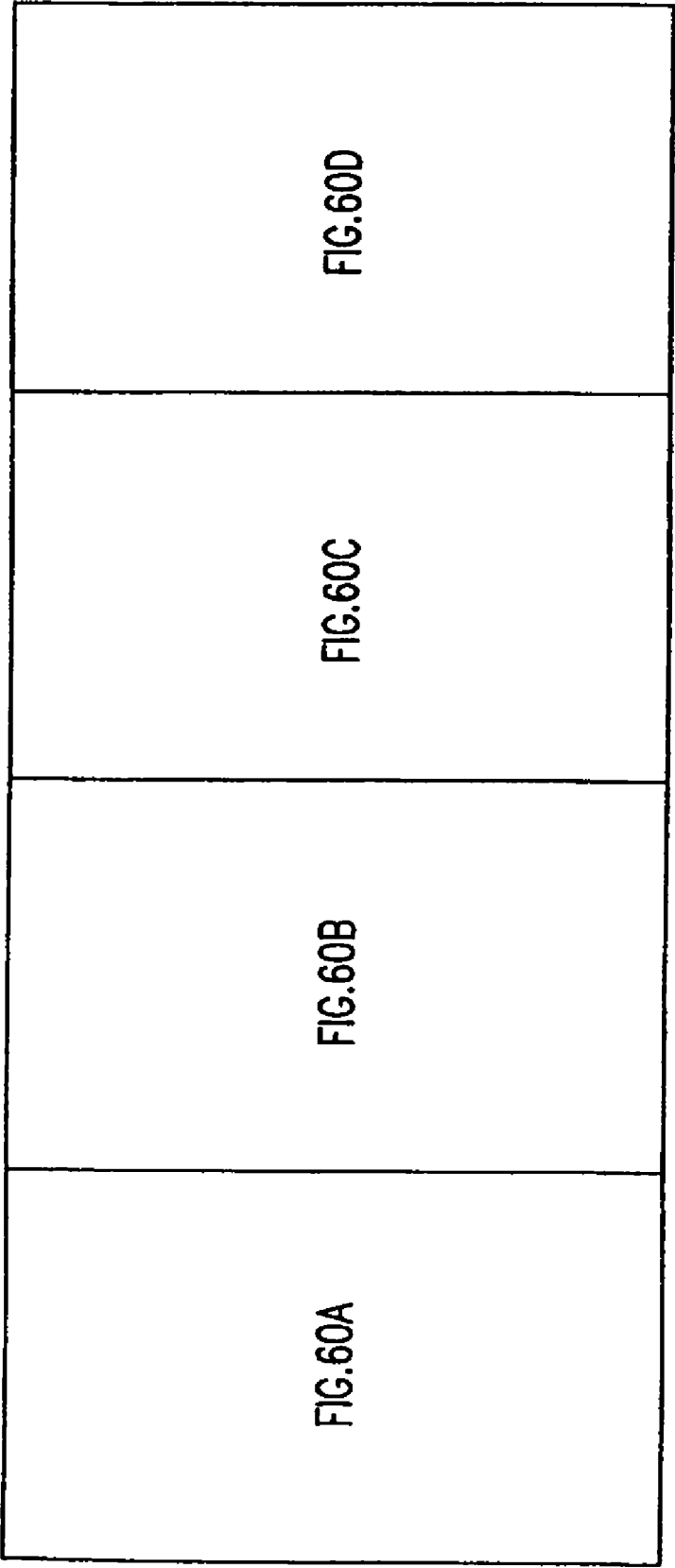


FIG. 60

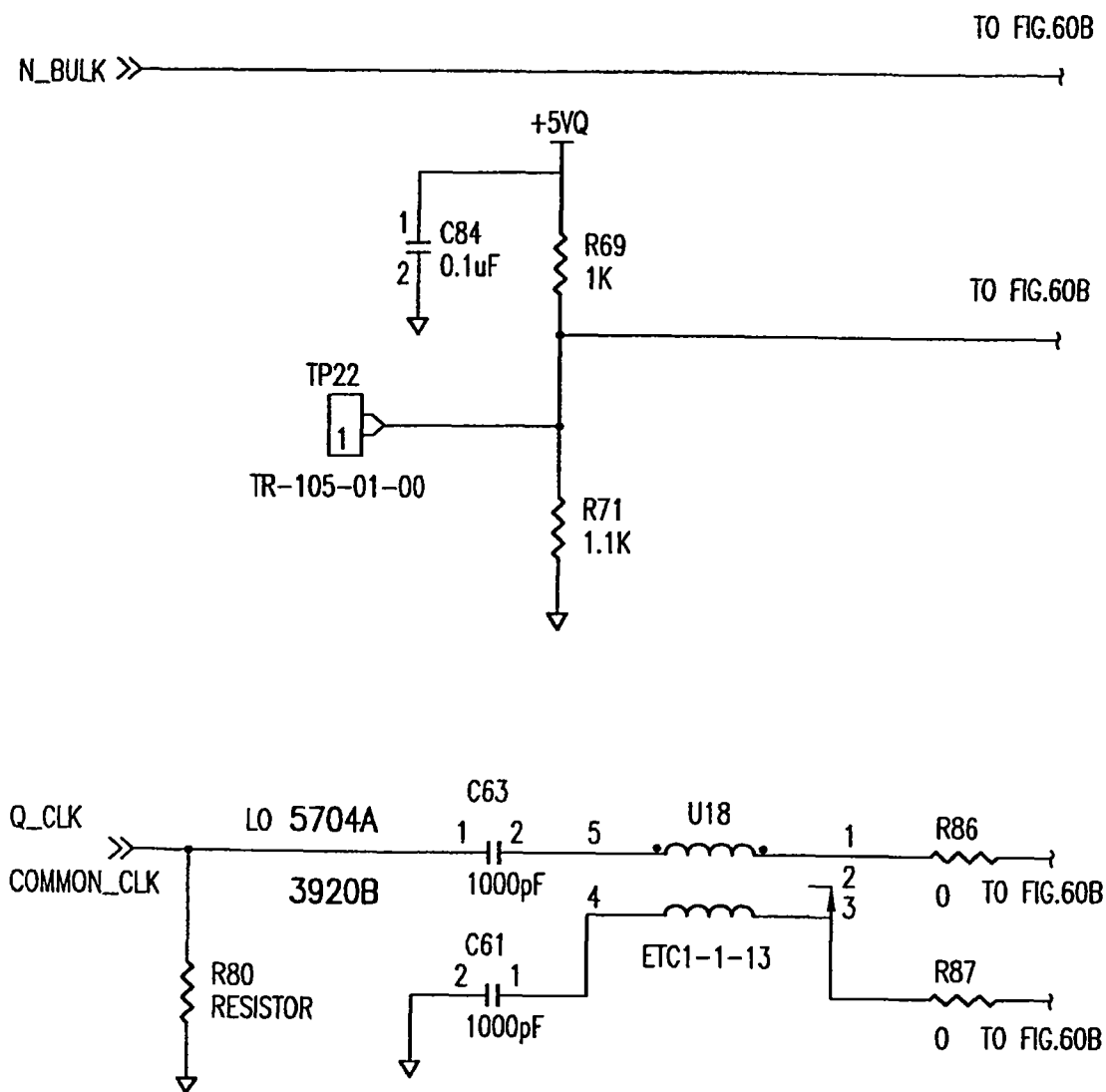


FIG.60A

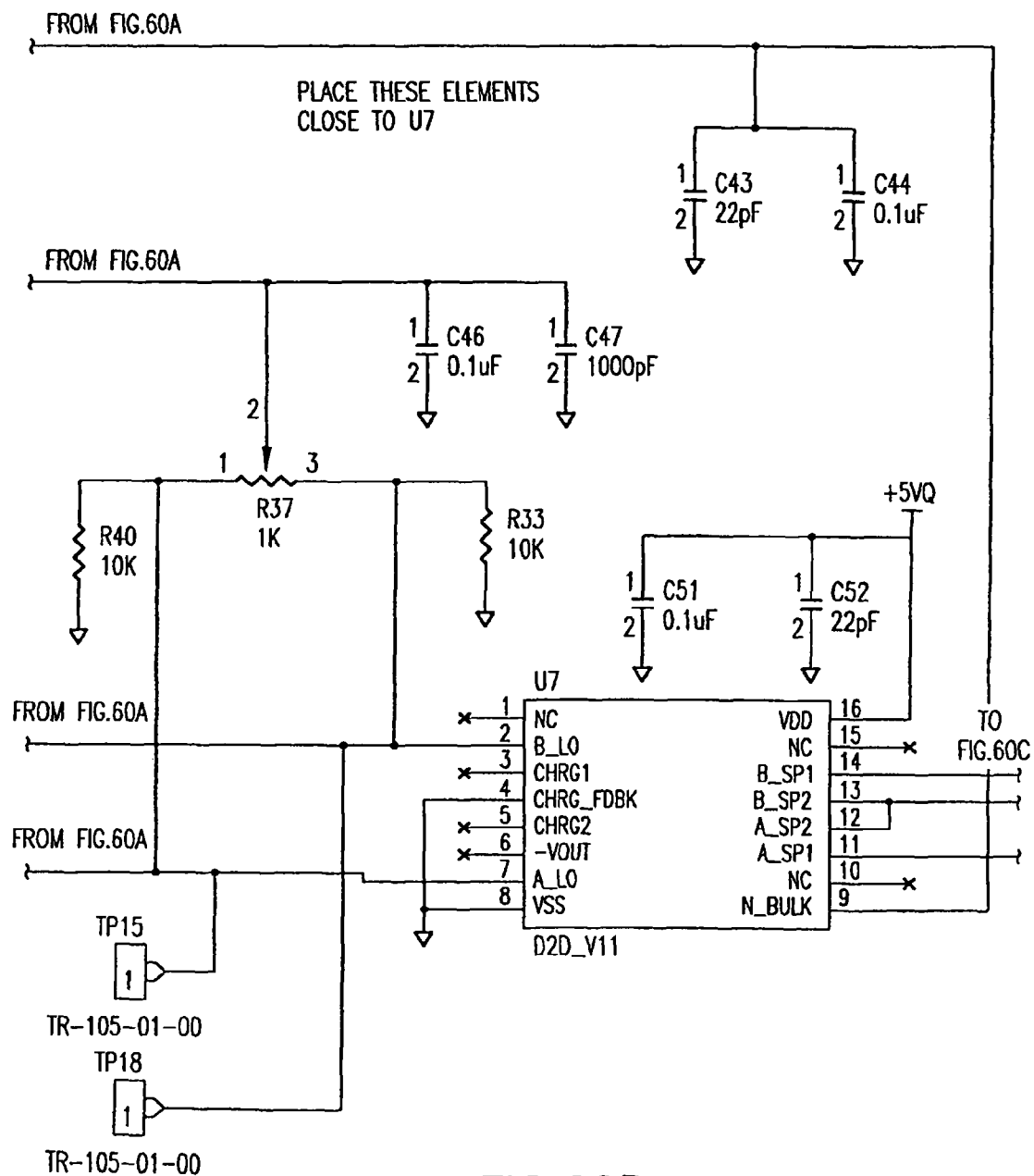


FIG. 60B

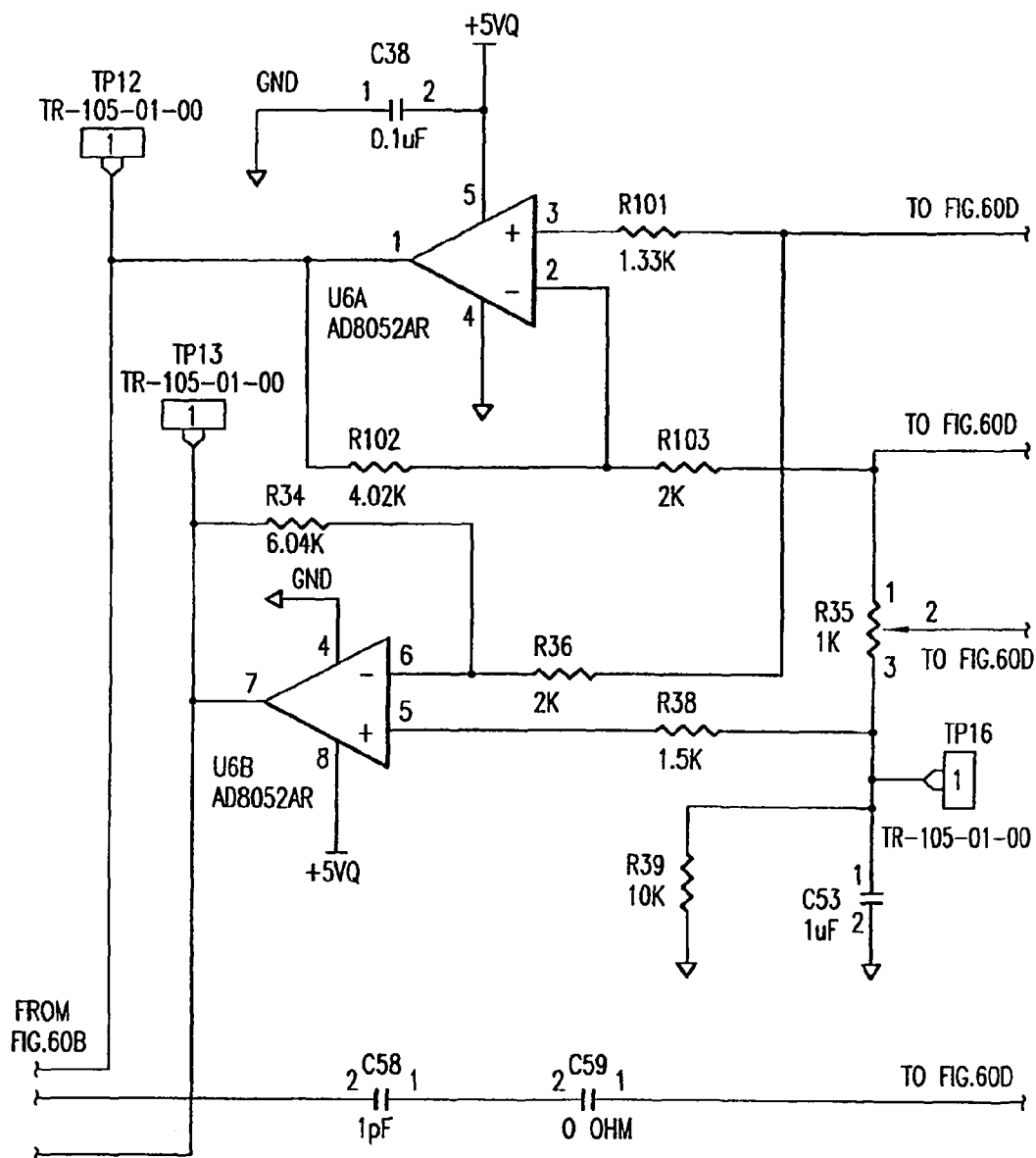


FIG. 60C

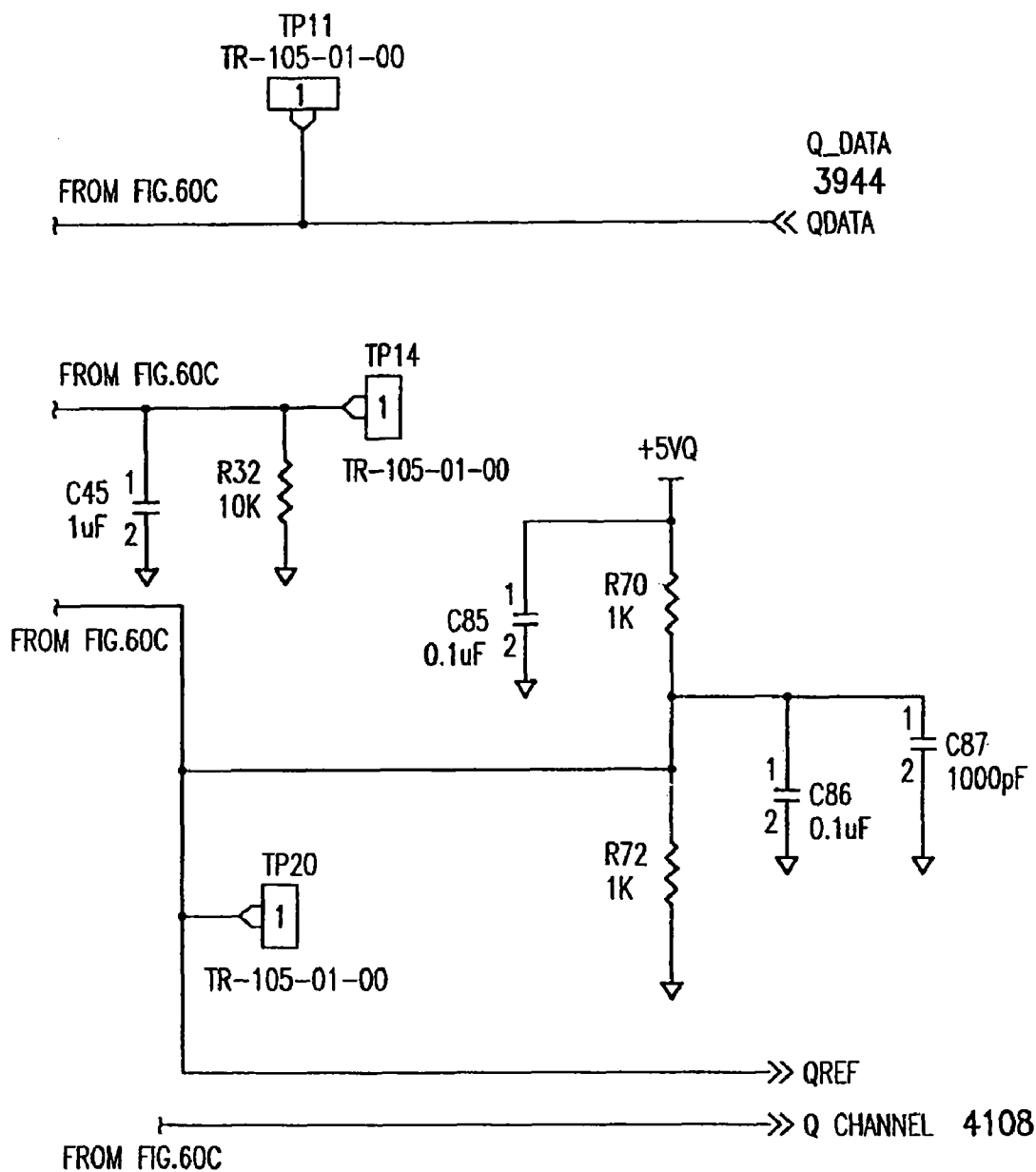


FIG.60D

ITEM	QTY	REFERENCE	PART	PART NUMBER	MANUFACTURER
1	21	C3, C6, C8, C10, C14, C38, C44, C46, C51, C71, C72, C77, C78, C79, C84, C85, C86, C93, C95, C96, C98	0.1uF	GRM39XR104K016	MURATA
2	6	C5, C7, C15, C43, C52, C75	22pF	GRM39CG220J050	MURATA
3	5	C9, C16, C45, C53, C89	1uF	GRM40V5V105Z016	MURATA
4	8	C11, C23, C25, C47, C61, C63	1000pF	GRM39XR102K050	MURATA
5	2	C80, C87			
6	2	C58, C21	1pF	GRM39CG010B50V	MURATA
7	2	C82, C33	4.7uF	T491A475K006AS	KEMET
8	1	C59, C35	0 ohm	GRM39CG0xxx50V	MURATA
9	1	C73	470pF	GRM39CG471J050	MURATA
10	3	C83	1uF	T491A105M016AS	KEMET
11	2	C90, C91, C92	100pF	ECU-V1H101JCV	
12	1	C94, C97	0.01uF	GRM39XR103K016	MURATA
13	1	FL1	MDR642E	MDR642E	SOSHIN
14	1	JP1	Shunt	69190-402	BERG
15	4	JP2	69190-403	69190-403	BERG
16	1	J7, J8, J9, J10	82MCMX-50-0-1	82MCMX-50-0-1	SUHER
17	1	L10	22nH	LL1608-F22NK	COILCRAFT
18	1	L12	BLM11A121S	BLM11A121S	MURATA
19	10	L13	330nH	LL2012-FR33K	
20	2	R5, R6, R12, R13, R32, R33, R39, R40, R95, R100	10K	ERJ3EKF1002	PANASONIC
21	4	R34, R7	6.04K	ERJ3EKF6041	PANASONIC
22	4	R8, R10, R35, R37	1K	3224W-1-102	BOURNS
23	2	R9, R36, R90, R103	2K	ERJ3EKF2001	PANASONIC
24	3	R38, R11	1.5K	ERJ3EKF1501	PANASONIC
		R56, R94, R99	0 ohm	ERJ3G5V0R00	PANASONIC

FIG. 61A

25	1	R59	51	ERJ3G5YJ510	PANASONIC
26	7	R60, R61, R62, R84, R85, R86, R87	0	ERJ3G5YOR00	PANASONIC
27	6	R63, R64, R66, R69, R70, R72	1K	ERJ3EKF1001	PANASONIC
28	2	R71, R65	1.1K	ERJ3EKF1101	PANASONIC
29	2	R80, R79	RESISTOR		
30	3	R81, R82, R83	R		
31	4	R88, R91, R96, R101	1.33K	ERJ3EKF1331	PANASONIC
32	2	R102, R89	4.02K	ERJ3EKF4021	PANASONIC
33	2	R92, R97	499	ERJ3EKF4990	PANASONIC
34	19	TP1, TP2, TP3, TP4, TP5, TP6, TP8, TP9, TP11, TP12, TP13, TP14, TP15, TP16, TP18, TP19, TP20, TP21, TP22	TP-105-01-00		
35	3	U1, U6, U19	AD8052AR	AD8052AR	ANALOG DEVICES
36	2	U7, U2	D2D_V11	D2D_V11	PARKER VISION
37	1	U11	MAAM22010	MAAM22010	MACOM
38	1	U12	1X603	1X603	ANAREN
39	1	U14	AD1582	AD1582	ANALOG DEVICES
40	1	U15	UPG1678	UPG1678GV	NEC
41	1	U16	ADP-2-10-75	ADP-2-10-75	MINI-CIRCUITS
42	1		BOARD	8500.641.021	V05.10

FIG. 61B

FIG.62A	FIG.62B
FIG.62C	FIG.62D
FIG.62E	FIG.62F
FIG.62G	FIG.62H
FIG.62I	

FIG. 62



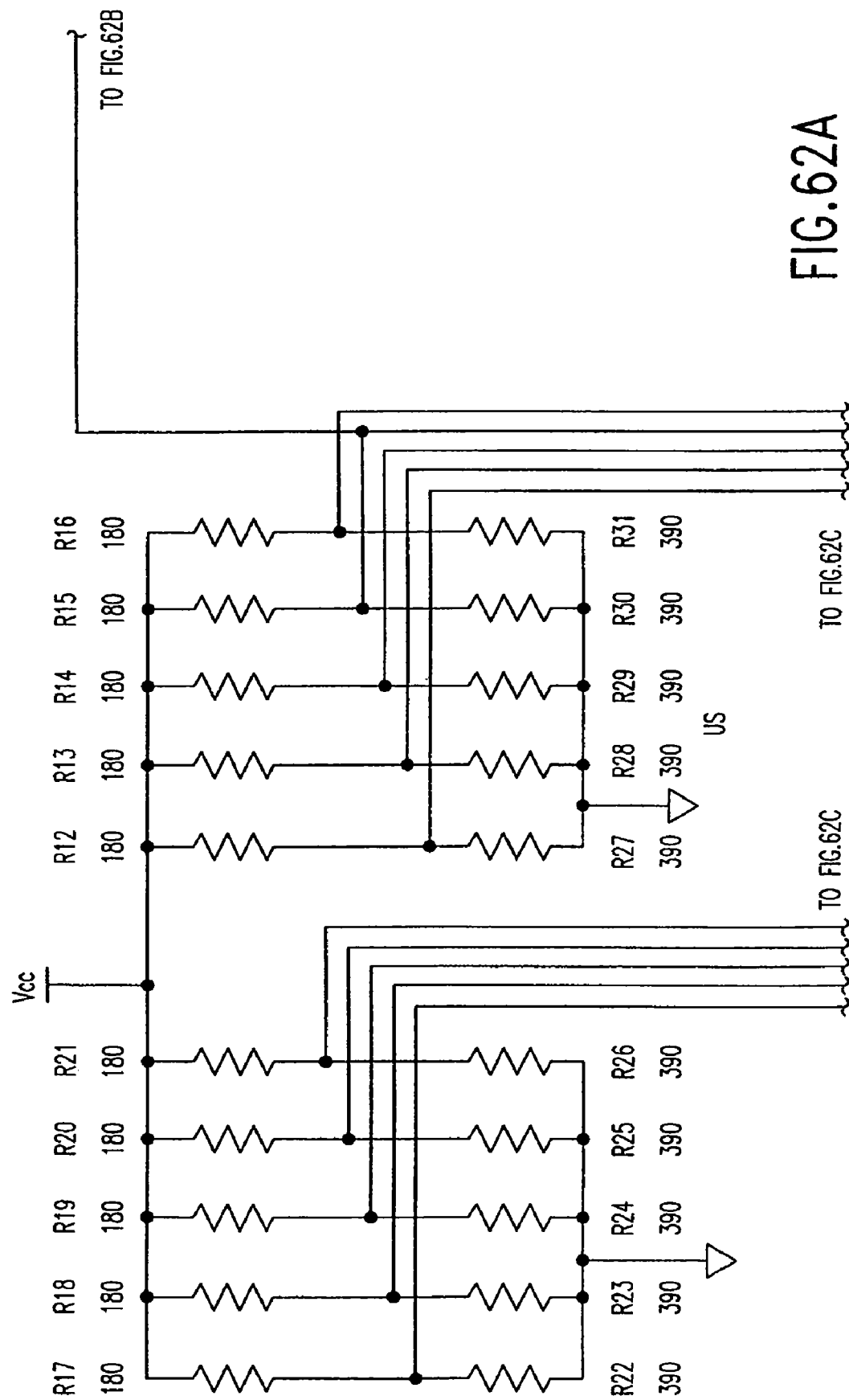
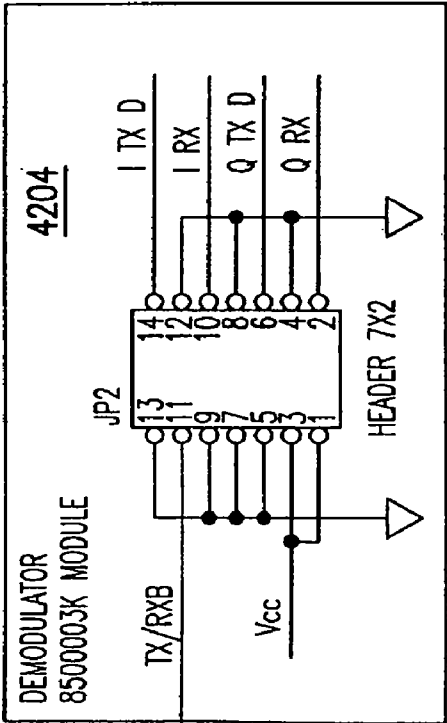
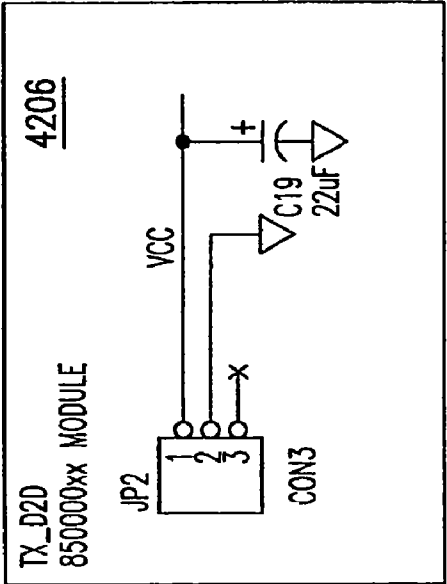


FIG. 62A



FROM FIG. 62A

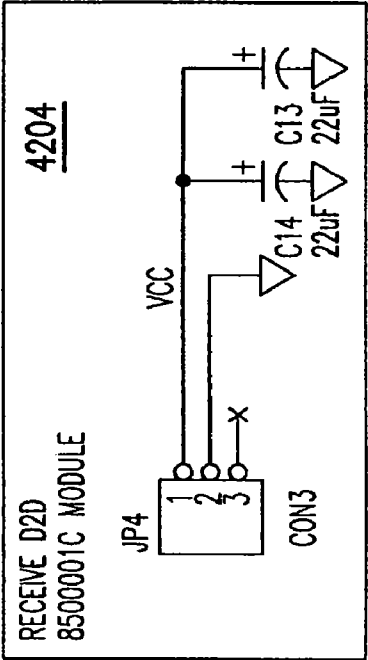


FIG. 62B

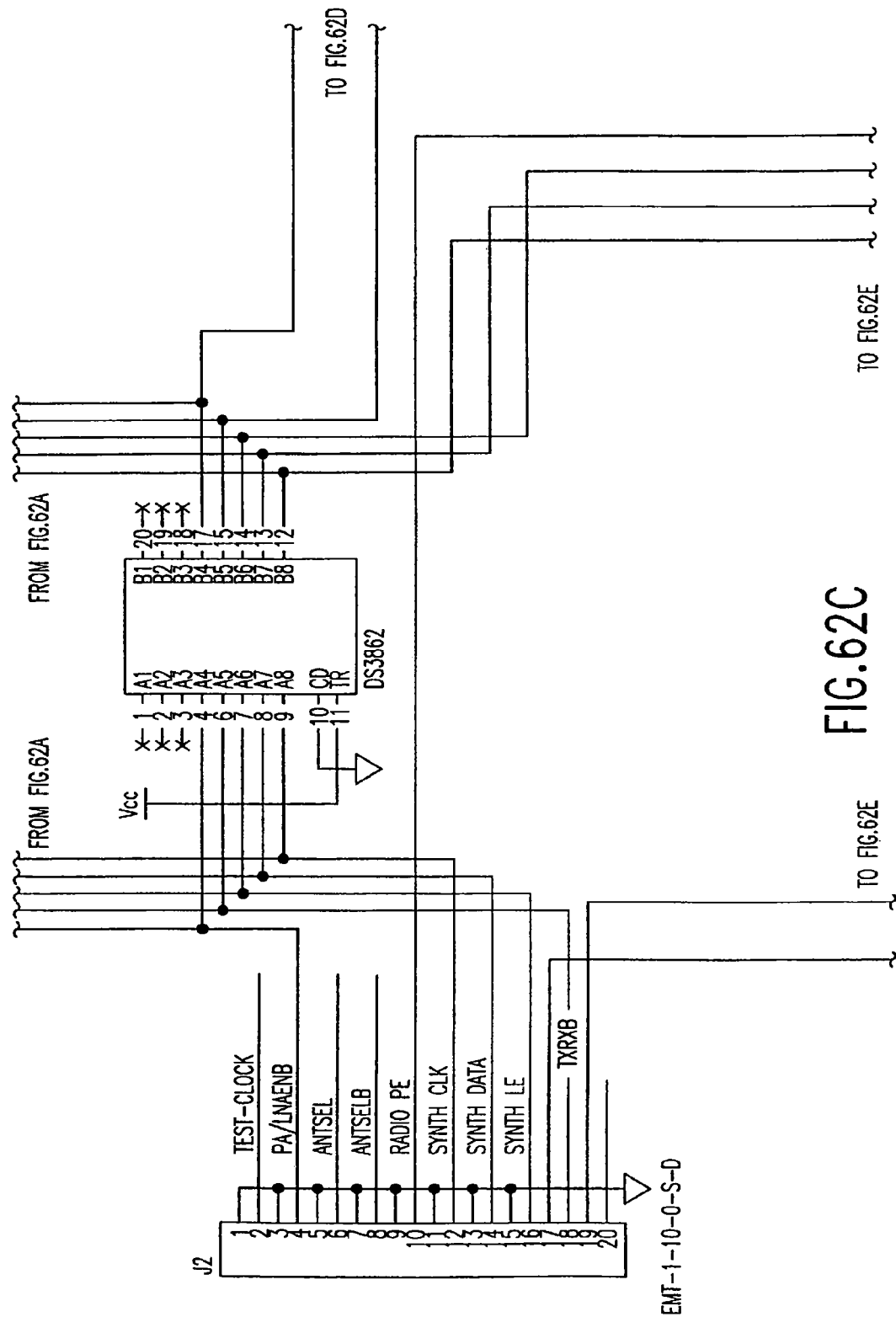


FIG. 62C

LNA/PA  
8500002C MODULE  
4212

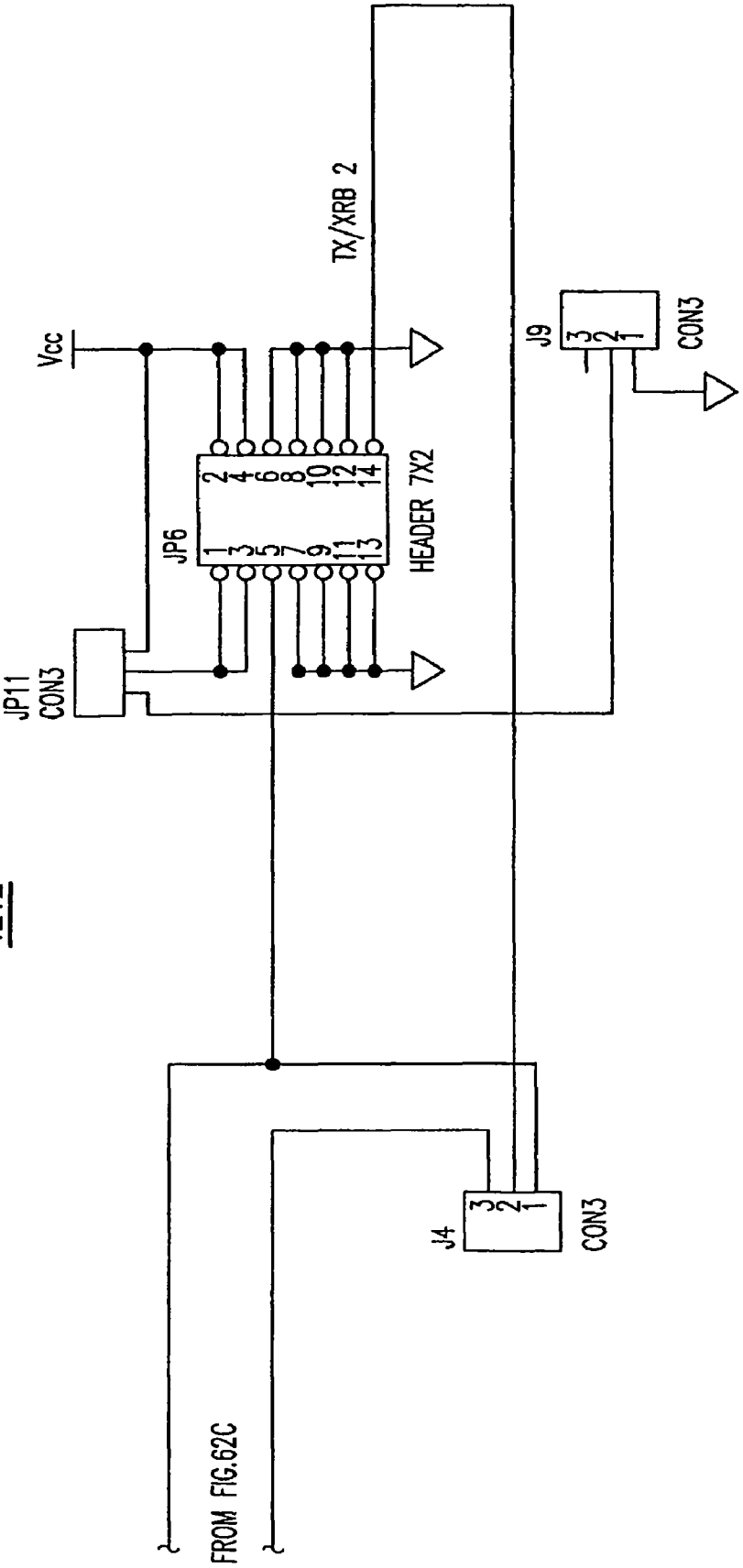
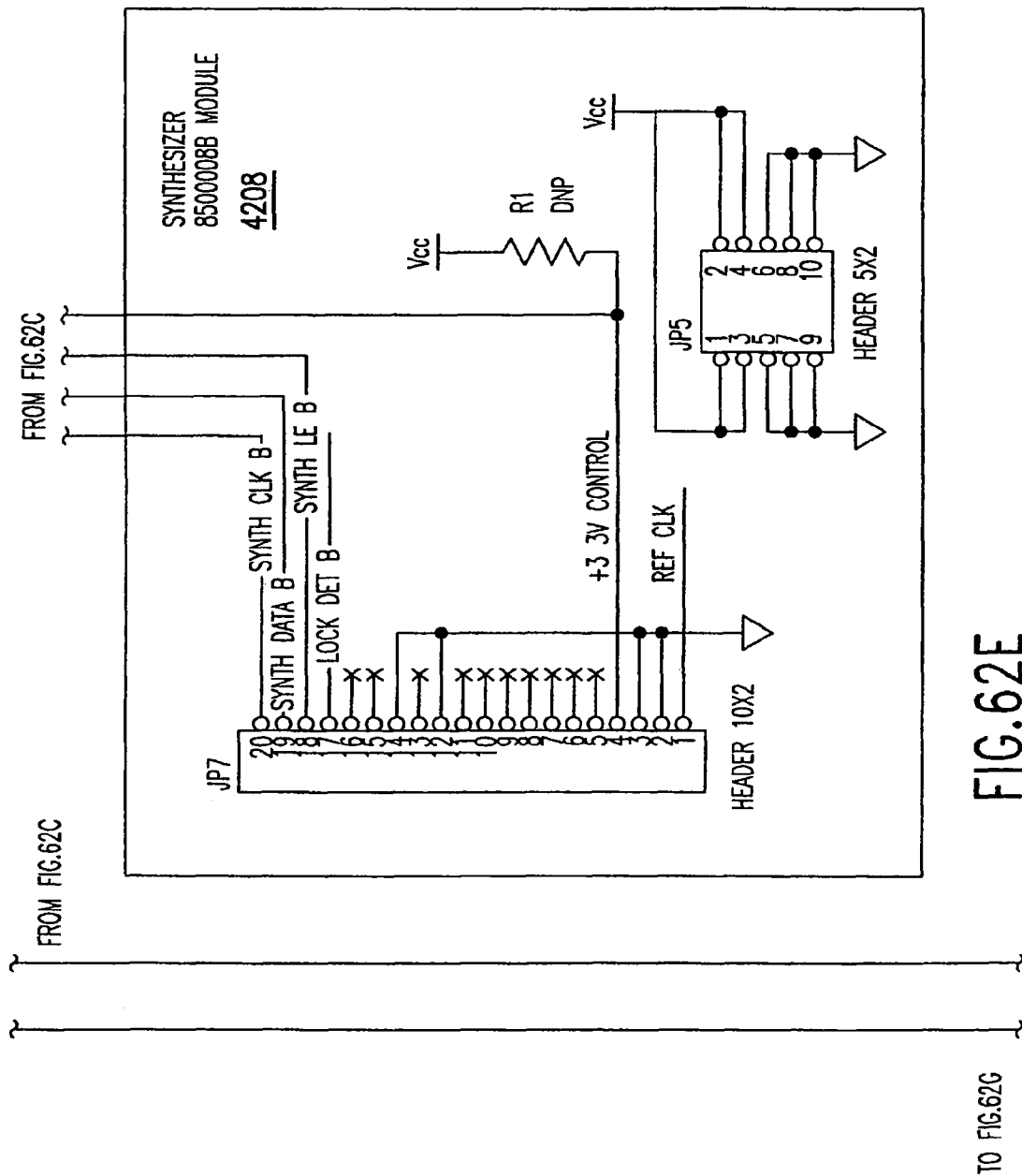


FIG. 62D



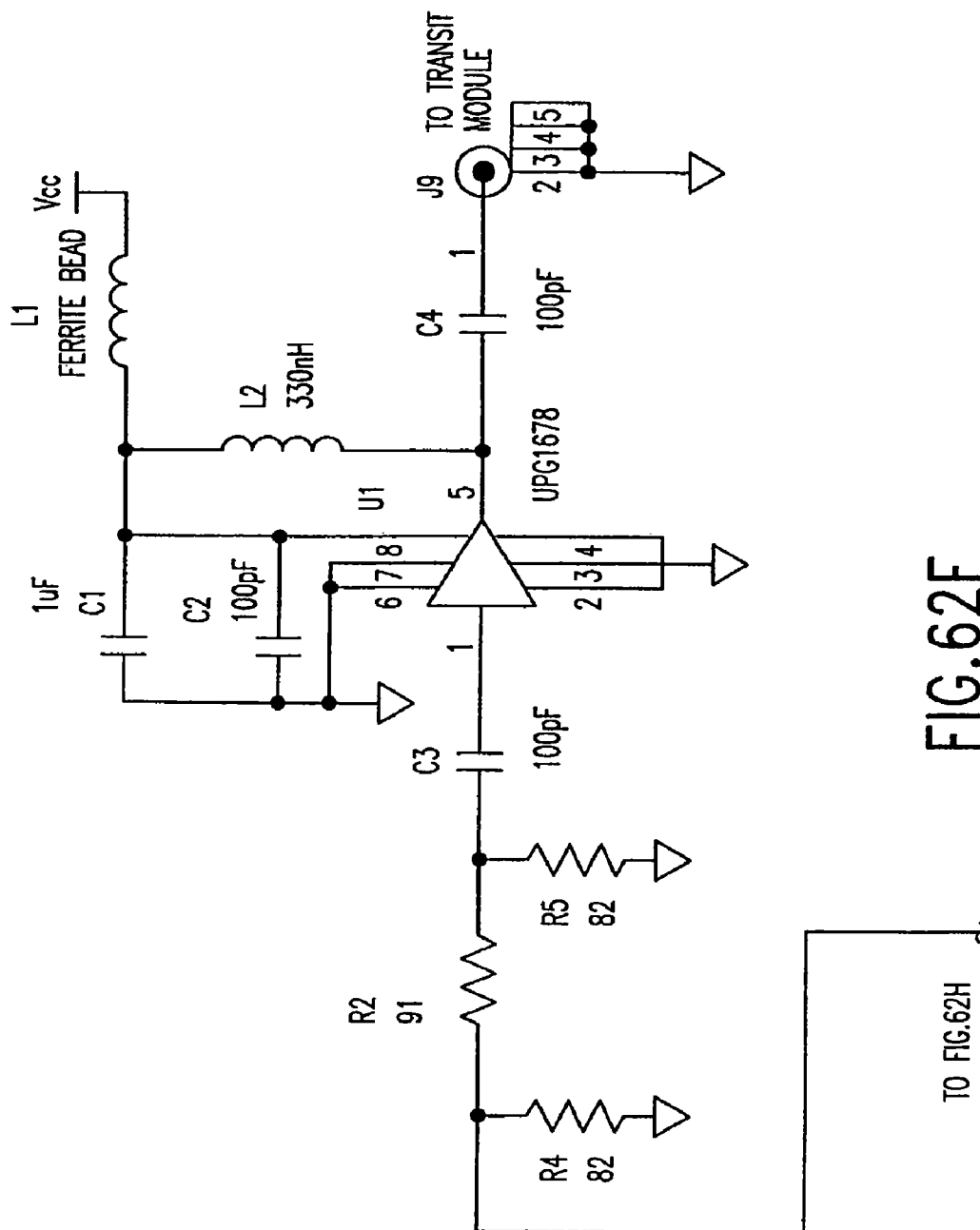
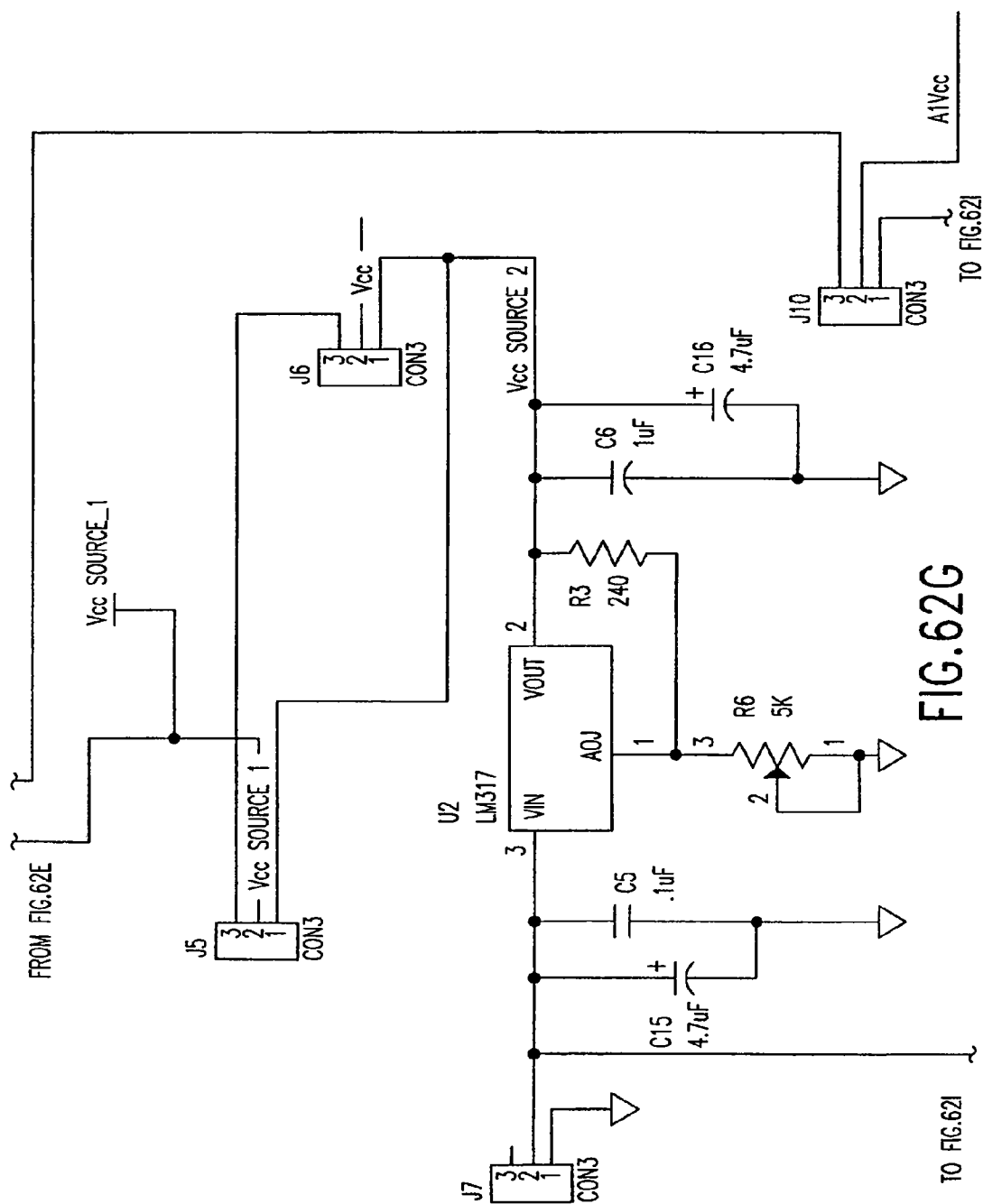


FIG. 62F



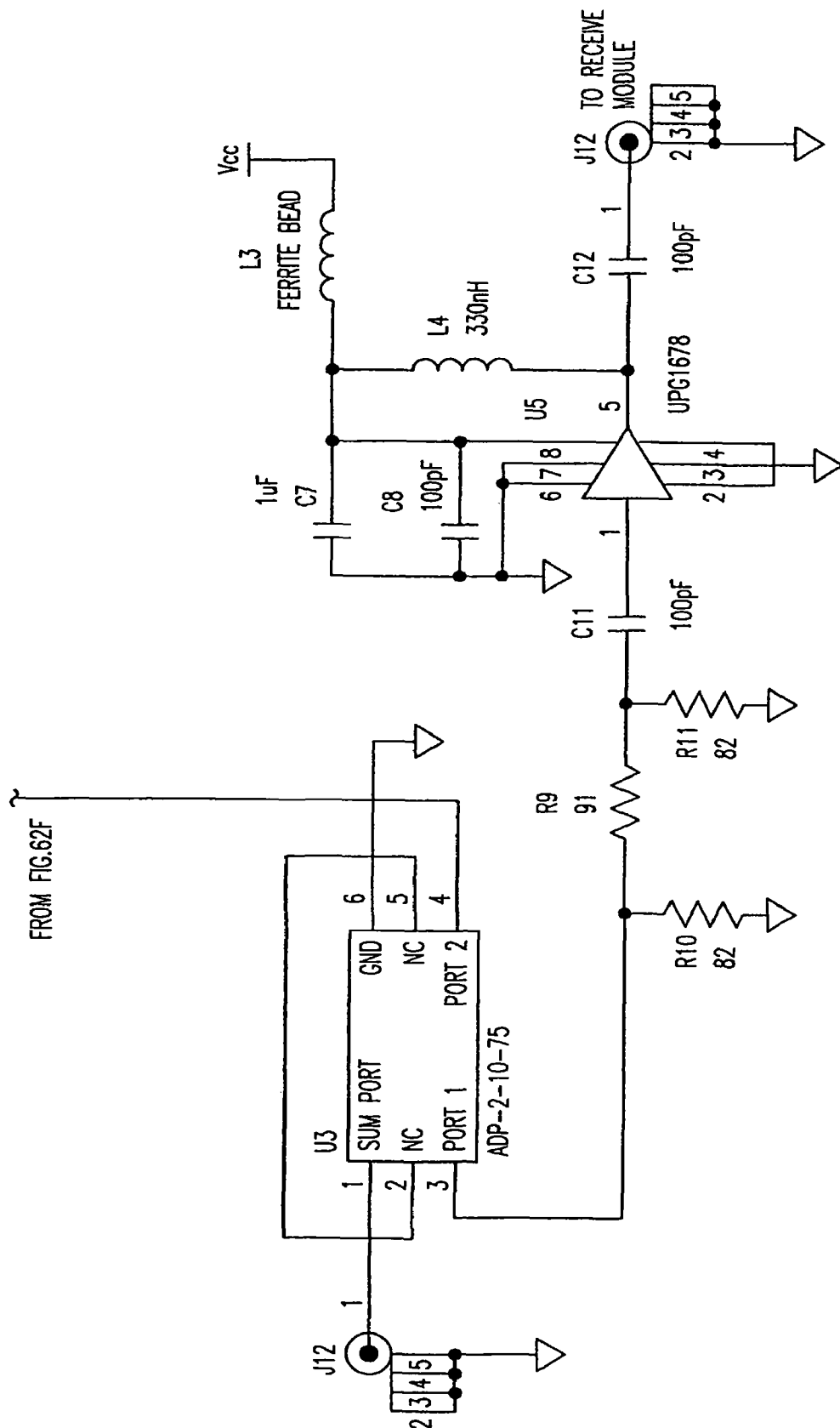


FIG. 62H



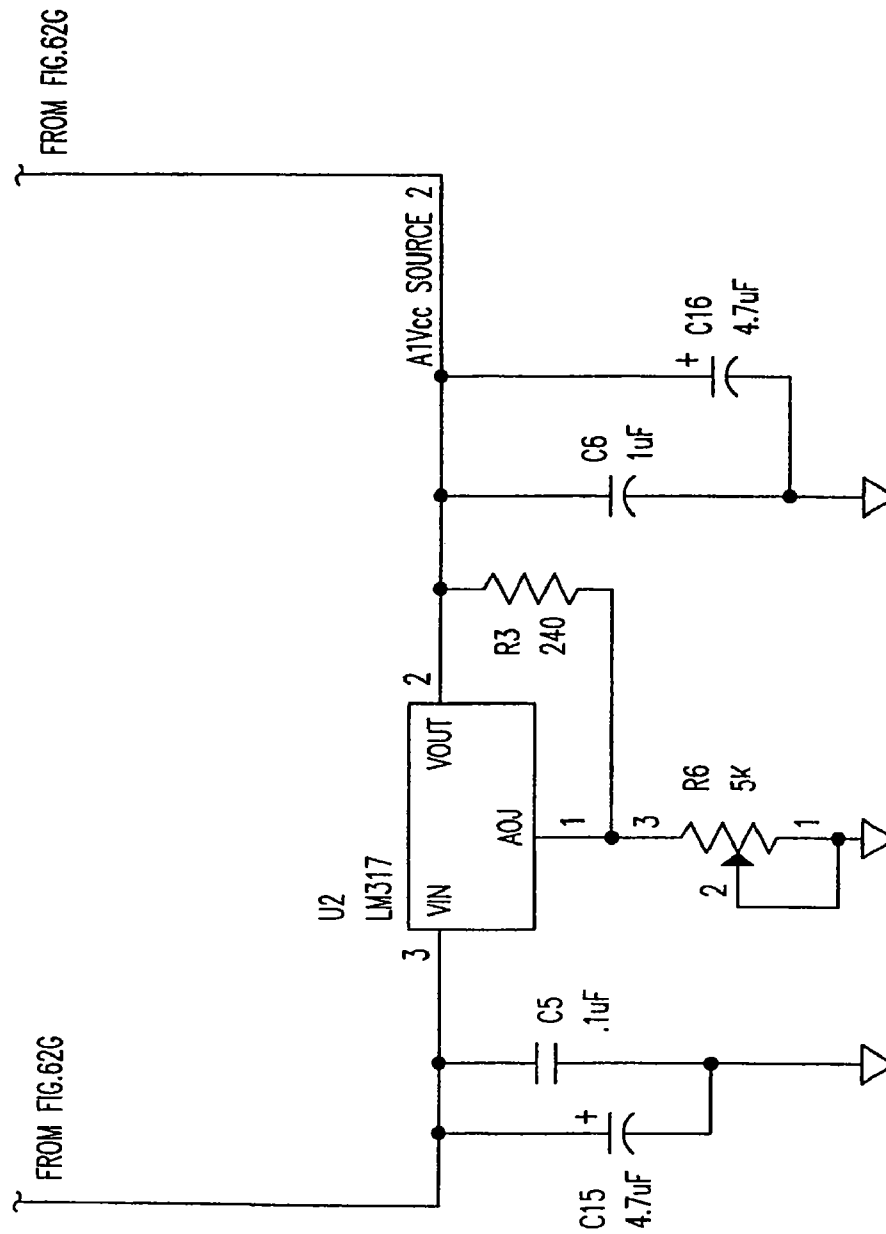


FIG. 62I

ITEM/QTY/REFERENCE	PART	DESCRIPTION	PART NUMBER	VENDOR
1 4 C1,C6,C7,C10	1uF	Cap, 1uF, +80-20%, 0805	GRM40Y5V105Z016AD	MURATA
2 6 C2,C3,C4,C8,C11,C12	100pF	Cap, 100pF, 5%, C0G, 0603	ECU-V1H101JCV	PANASONIC
3 2 C5,C9	.1uF	Cap, .1uF, +80-20%, Y5V, 0603		MURATA
4 3 C13,C14,C19	22uF	Cap, Tant, 22uF, 20%, 20V	T491D226M020AS	KEMET
5 4 C15,C16,C17,C18	4.7uF	Cap, Tant, 4.7uF, 20%, 20V	T491C475M020AS	KEMET
6 2 JP2,JP6	HEADER 7X2	Receptacle, 7x2pin, .050	SFMC-107-L1-S-D	SAMTEK
7 9 JP4, J4, J5, J6, J7, JP9, J9, CON3		Header, 3pin, .100"	69190-403	BERG
8 1 JP7	HEADER 10X2	Receptacle, 10X2pin, .050	SFMC-110-L1-S-D	SAMTEK
9 1 JP8	HEADER 5X2	Receptacle, 5X2pin, .050	SFMC-105-L1-S-D	SAMTEK
10 1 J2	EHT-1-10-01-S-D	Header, ribbon, 10X2pin, 2mm	EHT-1-10-01-S-D	SAMTEK
11 3 J8, J11, J12	82MMCX-50-0-1	Connector, RF	82MMCX-50-0-1	SUHRER
12 2 L3, L1	Ferrite Bead	Ferrite Bead, 0805	BLM21A121S	MURATA
13 2 L4, L2	330nH	Ind, 330nH, 10%, 0805	LL2012-FR33K	TOKO
14 1 R1	ONP	Res, 0603		PANASONIC
15 2 R9, R2	91	Res, 91 Ohm, 5%, 0603	ERJ-36SYJ910	PANASONIC
16 2 R7, R3	240	Res, 240 Ohm, 5%, 0603	ERJ-36SYJ241	PANASONIC
17 4 R4, R5, R10, R11	82	Res, 82 Ohm, 5%, 0603	ERJ-36SYJ820	PANASONIC
18 2 R8, R6	5K	Var Res, 5K, 10%	3296W001502	BOURNS
19 10 R12, R13, R14, R15, R16, R17, R18, R19, R20, R21	180	Res, 180 Ohm, 5%, 0603	ERJ-36SYJ181	PANASONIC
20 10 R22, R23, R24, R25, R26, R27, R28, R29, R30, R31	390	Res, 390 Ohm, 5%, 0603	ERJ-36SYJ391	PANASONIC
21 2 U5, U1	UPG1678	IC, RF Buffer	UPG1678GV	NEC
22 2 U4, U2	LM317	IC, Voltage Regulator	LM317T	NATIONAL
23 1 U3	ADP-2-10-75	RF Splitter	ADP-2-10-75	MINICIRCUITS
24 1 U6	DS3862	IC, Buffer	DS3862NM	NATIONAL
25 1		BOARD	ST8500.641.023V0L01	

FIG.63

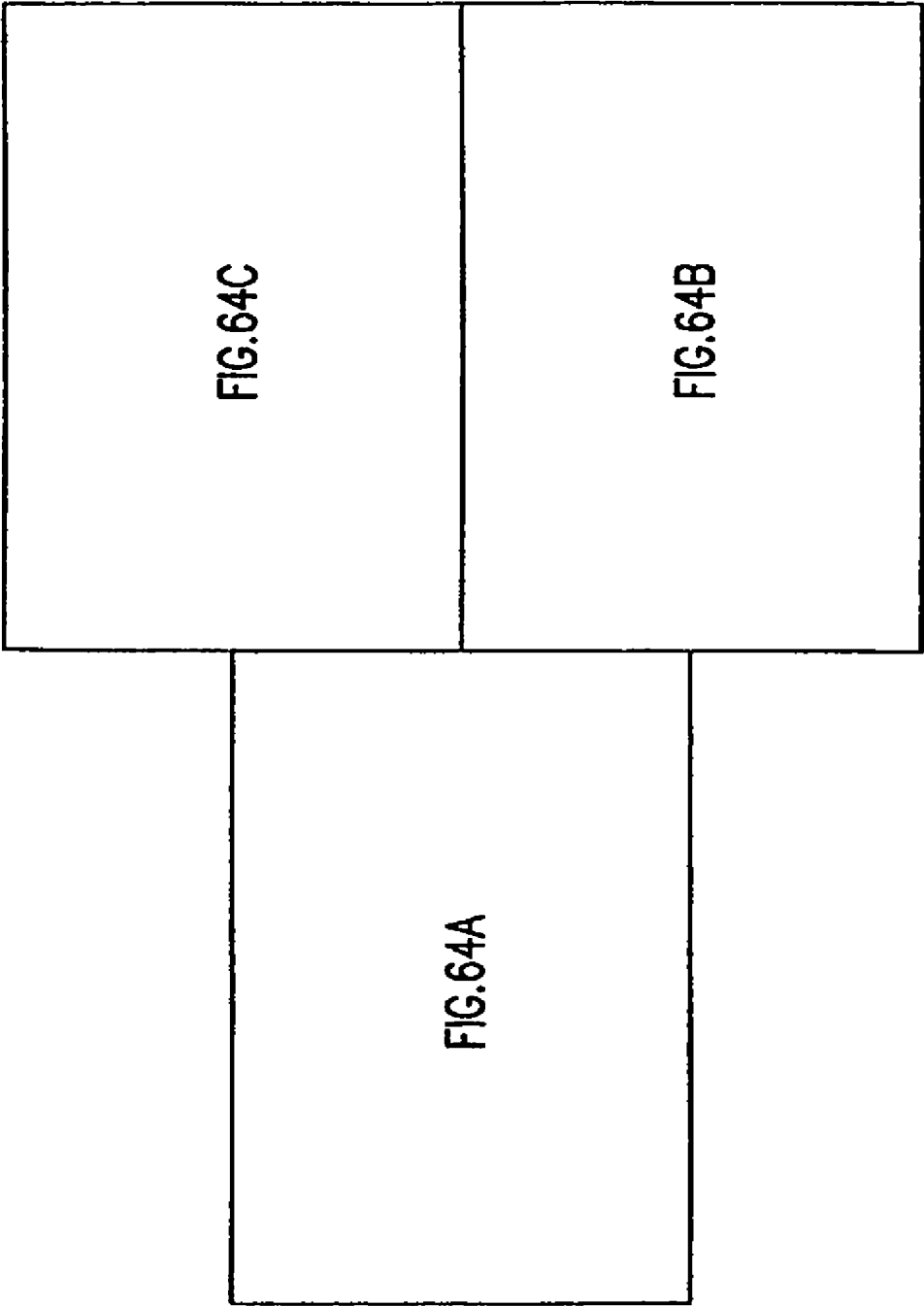
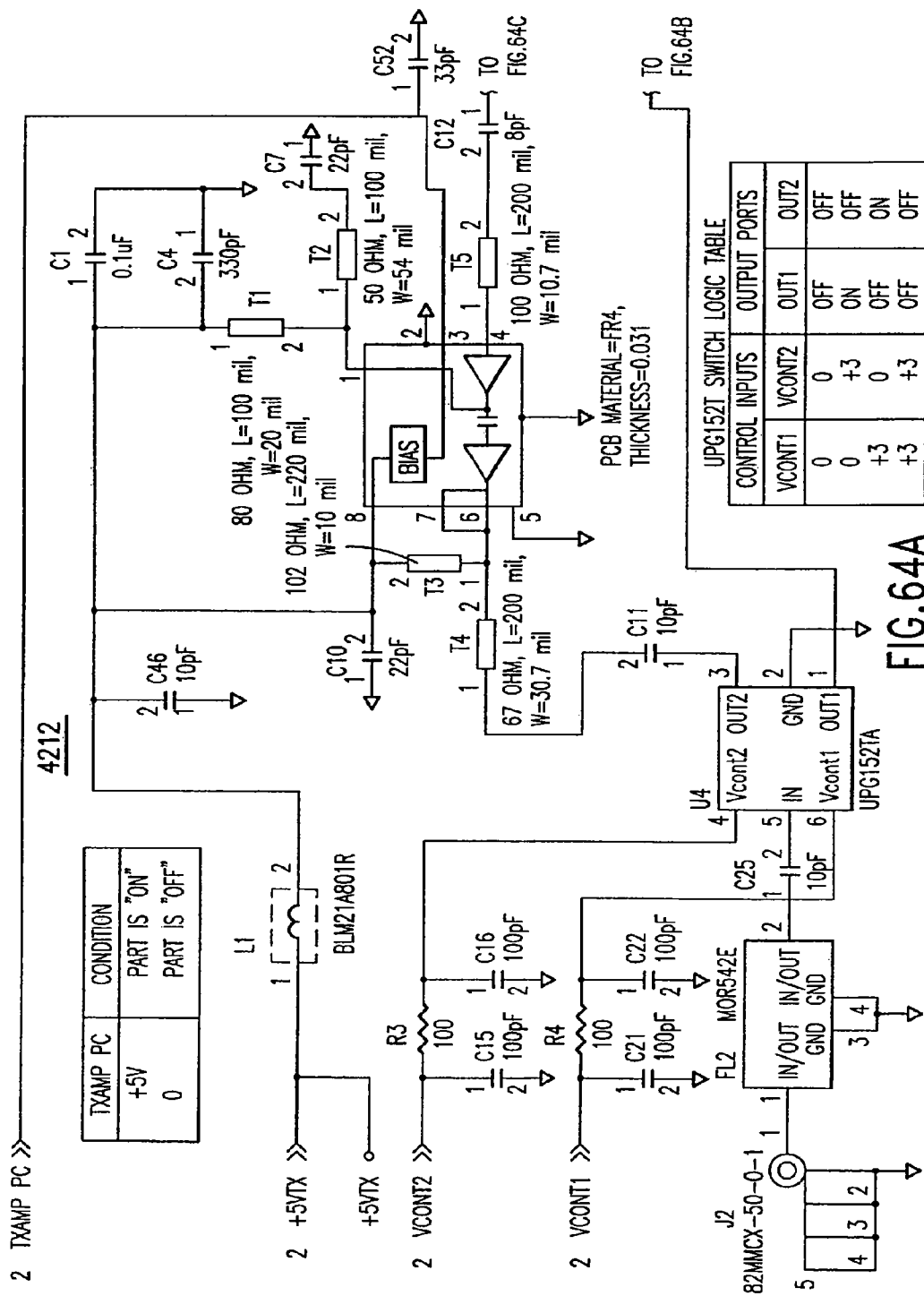
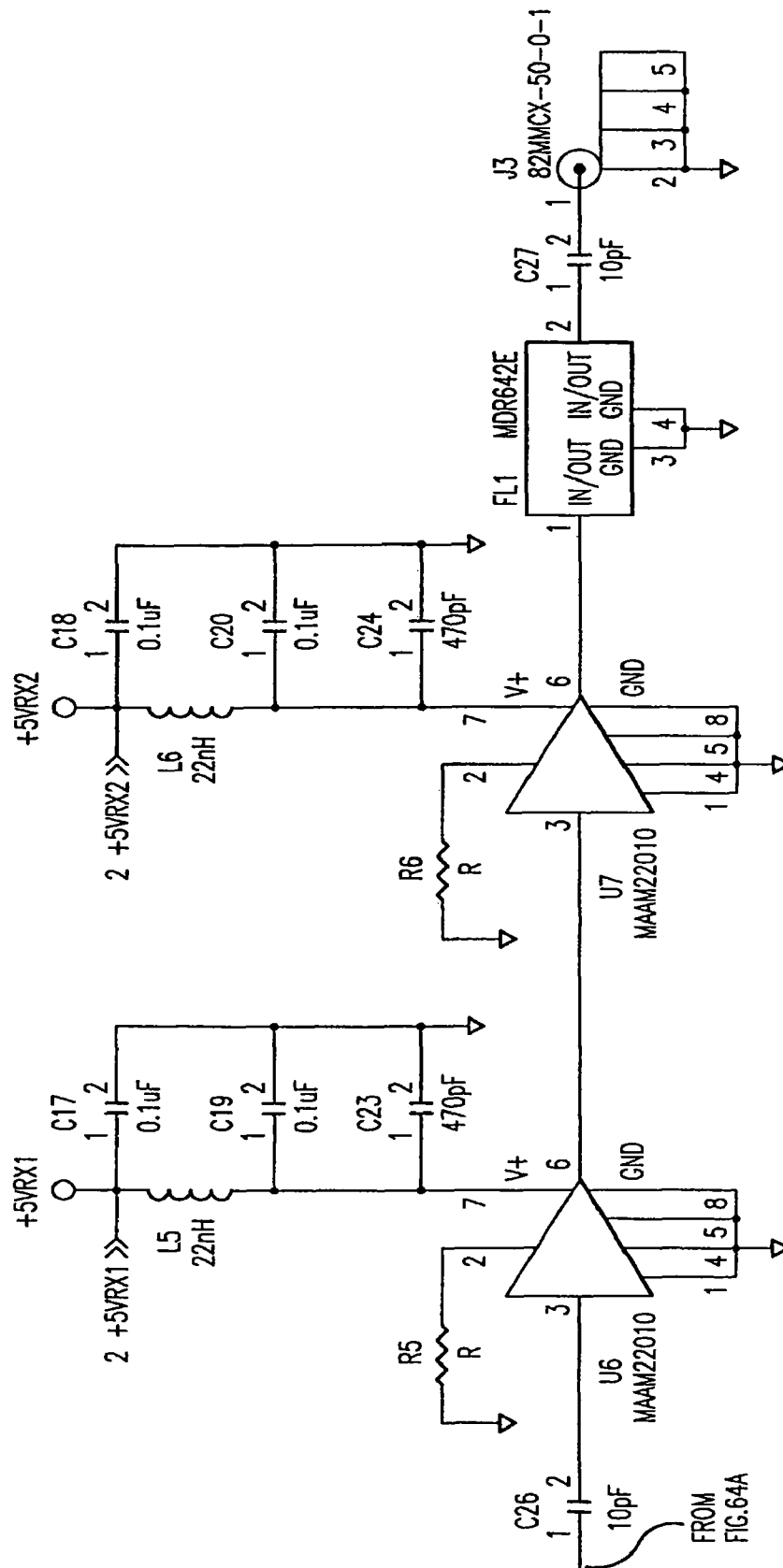
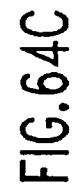


FIG. 64



**FIG. 64A**





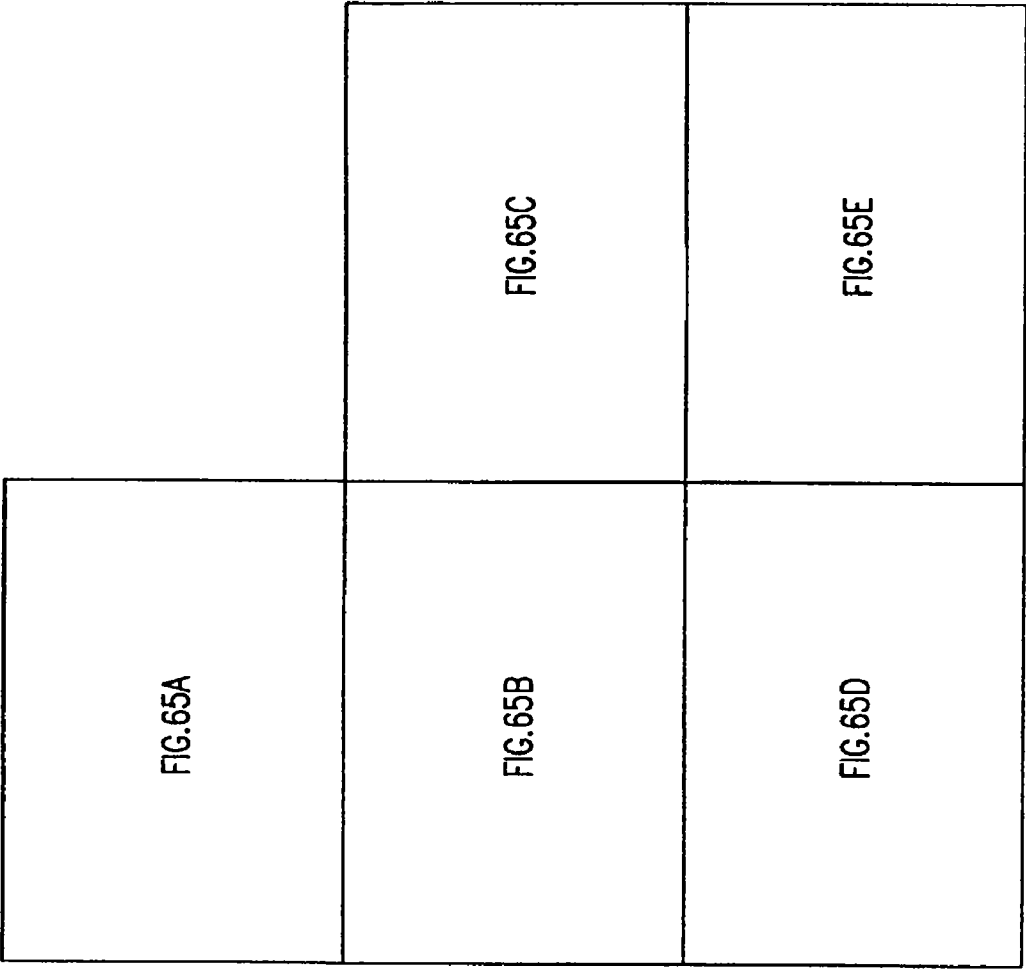


FIG. 65

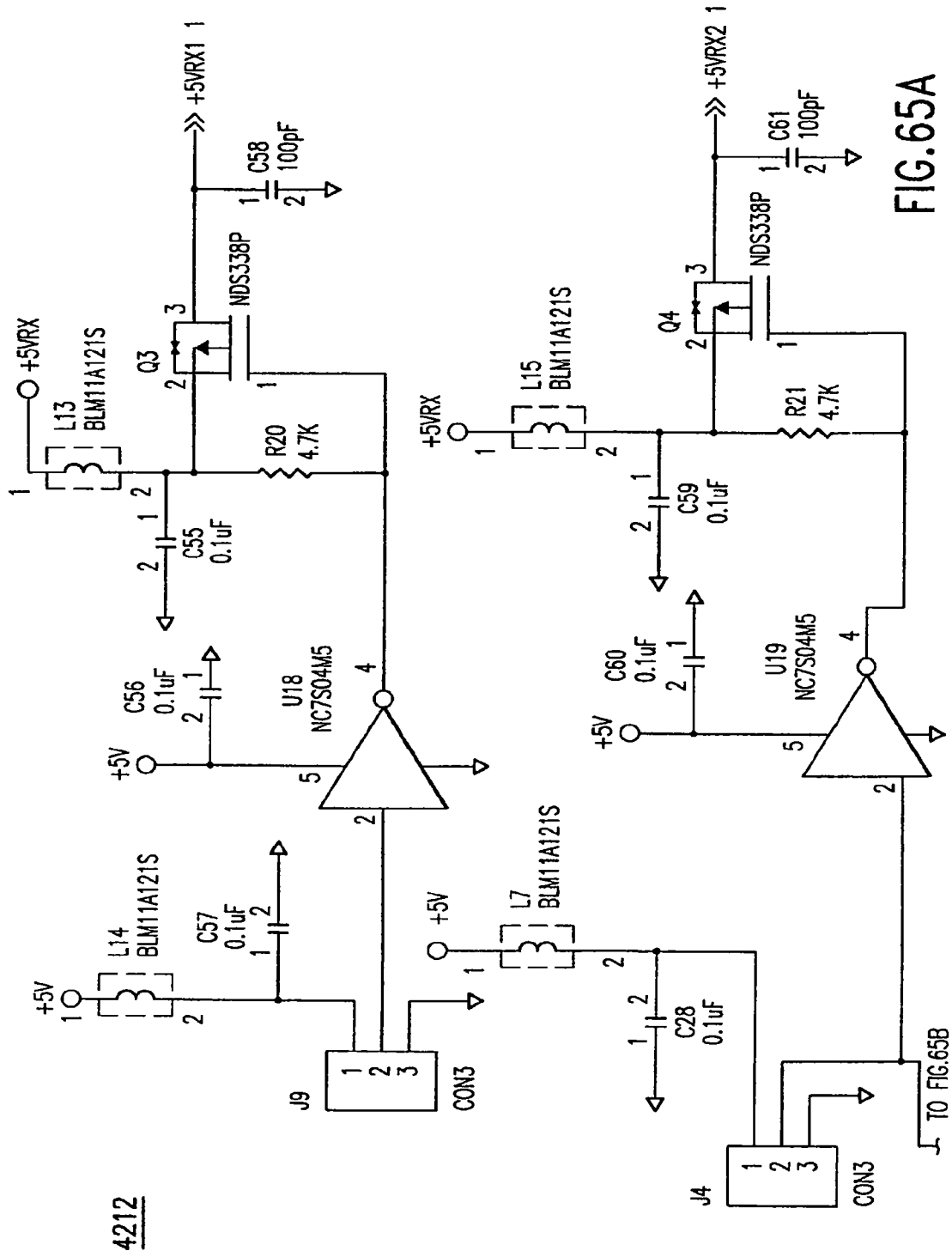
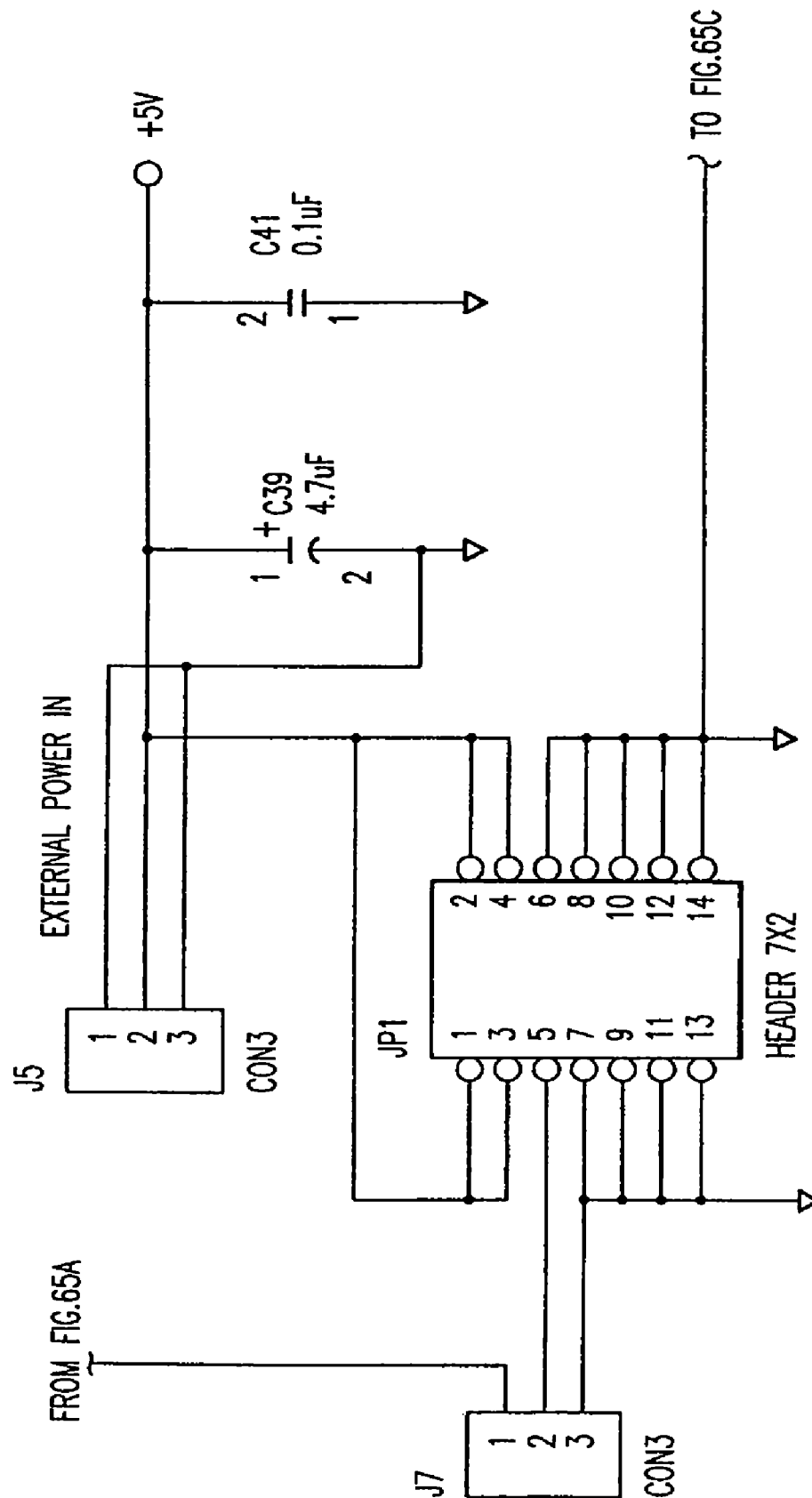


FIG. 65A





**FIG. 65B**

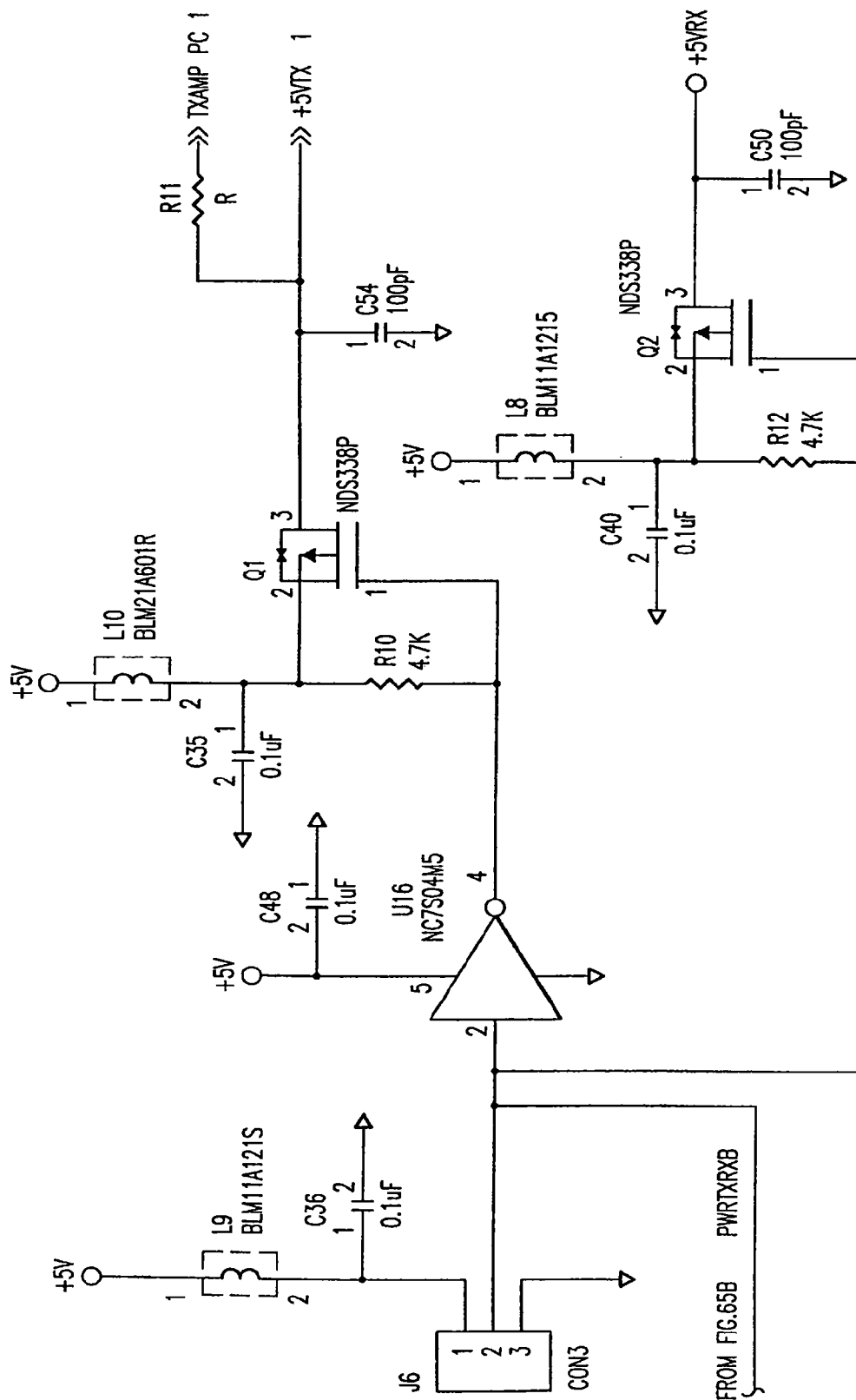


FIG. 65C

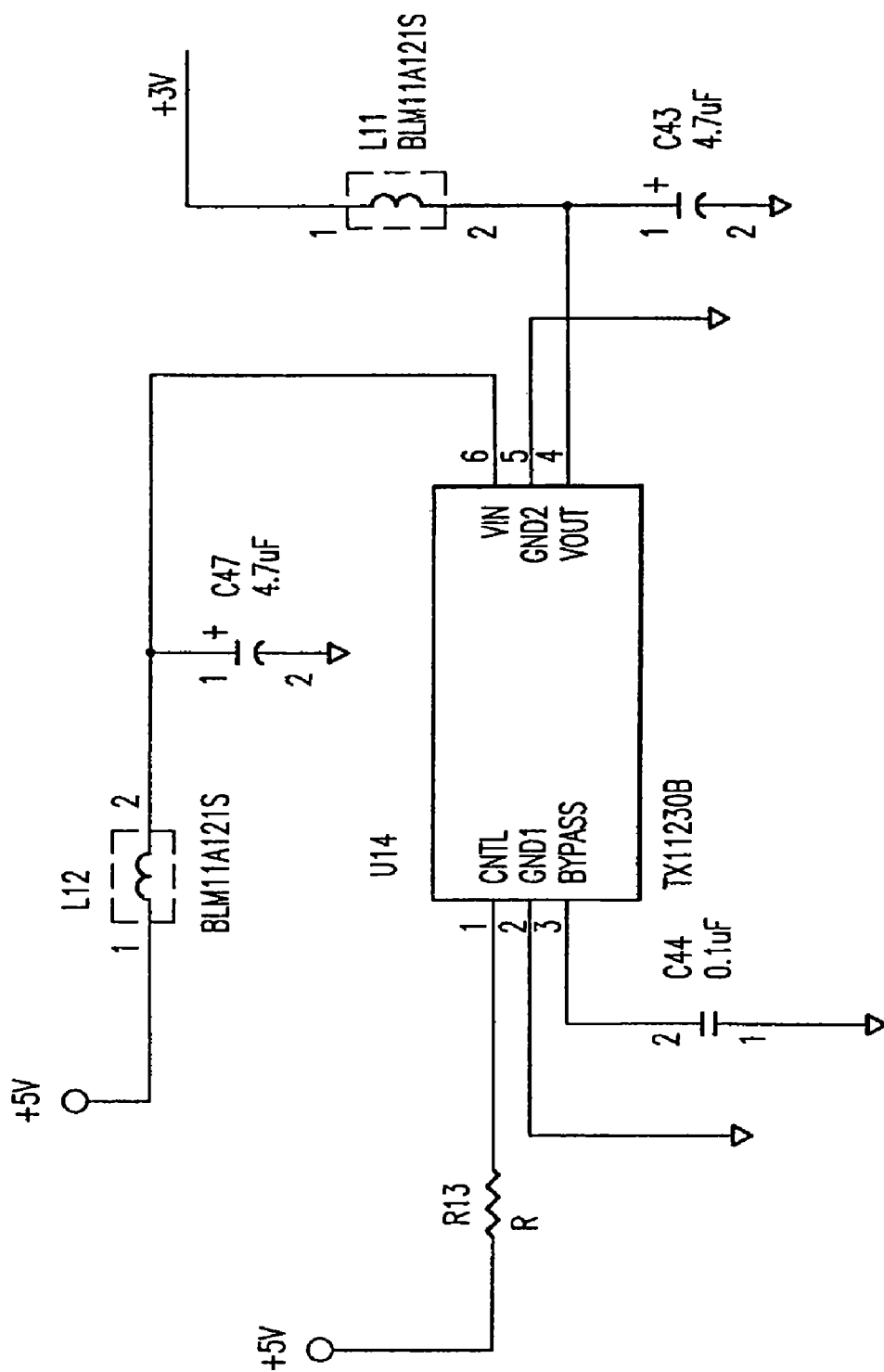


FIG. 65D

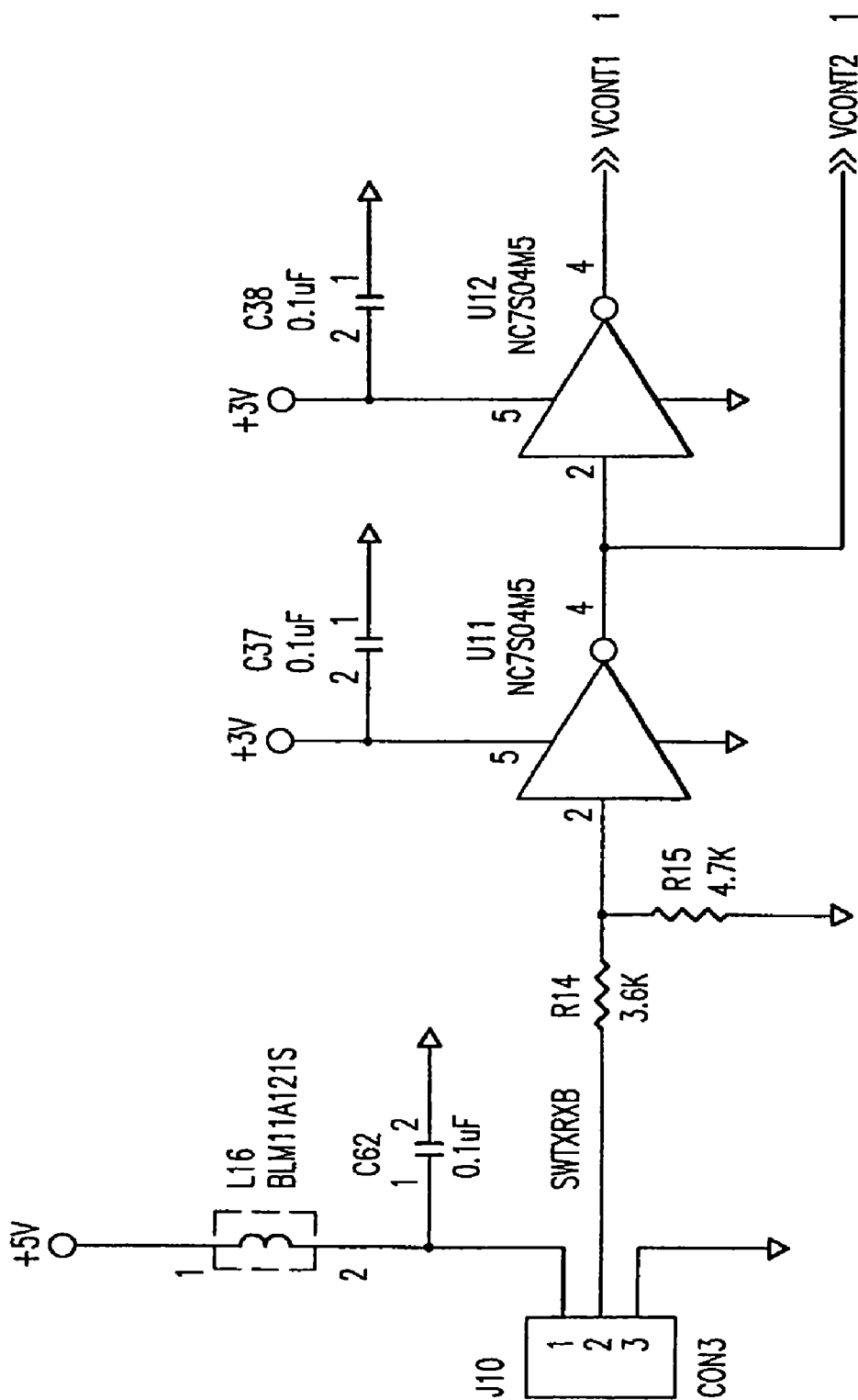


FIG. 65E

ITEM	QTY	REFERENCE	PART	MANUFACT.	PART DESCRIPTION	PART NUMBER
1	24	C1, C2, C3, C5, C6, C17, C18, C19, C20, C28, C35, C36, C37, C38, C40, C41, C44, C48, C55, C56, C57, C59, C60, C62	0.1uF	MURATA	.1uF, 0603, X7R, 20%, 16V	GRM39X7R104M016
2	1	C4	330pF	MURATA	330pF, 0603, COG, 10%, 50	GRM39COG331K050
3	2	C10, C7	22pF	MURATA	22pF, 0603, COG, 10%, 50	GRM30COG220K050
4	4	C8, C9, C23, C24	470pF	MURATA	470pF, 0603, COG, 10%, 50	GRM39COG471K050
5	6	C11, C13, C25, C26, C27, C46	10pF	MURATA	10pF, 0603, COG, 10%, 50	GRM39COG100K050
6	1	C12	8pF	MURATA	8pF, 0603, COG, 10%, 50	GRM39COG080K050
7	8	C15, C16, C21, C22, C50, C54	100pF	MURATA	100pF, 0603, COG, 10%, 50	GRM39COG101K050
8	3	C39, C43, C47	4.7uF	PANASONIC	4.7uF TANTALUM, 16V	ECS-T1CY475R
9	1	C52	33pF	MURATA	330pF, 0603, COG, 10%, 50	GRM30COG330K050
10	2	FL1, FL2	MDR642E	SOSHIN	2.4-2.5GHz BPF	MDR642E
11	1	JP1	HEADER 7X2	SAMTEC	DUAL ROW, 7 PINS PER ROW	FTSH-107-01-F-D
12	3	J1, J2, J3	82MCX-50-0-1	SUHER	RF CONNECTOR	82MCX-50-0-1
13	6	J4, J5, J6, J7, J9, J10	CON3	BERG	3 PIN HEADER W RETENTIVE LEG	69190-403H
14	2	L10, L1	BLM21A601R	MURATA	600 OHMS@100MHz, 500mA FERRITE BEAD	BLM21A601R
15	4	L2, L3, L5, L6	22nH	COILCRAFT	22nH, 0805CS (2012), 5%	0805CS-220X-BC
16	9	L7, L8, L9, L11, L12, L13, L14, L15, L16	BLM11A121S	MURATA	RF BEAD	BLM11A121S
17	4	Q1, Q2, Q3, Q4	NDS336P	NATIONAL	P-CHANNEL FET	NDS336P
18	12	R1, R2, R5, R6, R7, R9, R11, R13, R16, R17, R18, R19	R	PANASONIC		
19	2	R3, R4	100	PANASONIC	0603, 100, 5%, 1/16W	ERJ-3GSY-J-101
20	5	R10, R12, R15, R20, R21	4.7K	PANASONIC	0603, 4.7K, 5%, 1/16W	ERJ-3GSY-J-472

FIG. 66A

21	1	R14	3.6K	PANASONIC	0603, 3.6K, 5%, 1/16W	ERJ-3G5Y-J-362
22	1	T1	80 OHM, L=100 MIL, W=20 MIL		80 OHM, L=100 MIL, W=20 MIL	
23	1	T2	50 OHM, L=100 MIL, W=54 MIL		50 OHM, L=100 MIL, W=54 MIL	
24	1	T3	102 OHM, L=220 MIL, W=10 MIL		102 OHM, L=220 MIL, W=10 MIL	
25	1	T4	67 OHM, L=200 MIL, W=30.7 MIL		67 OHM, L=200 MIL, W=30.7 MIL	
26	1	T5	100 OHM, L=200 MIL, W=10.7 MIL		100 OHM, L=200 MIL, W=10.7 MIL	
27	4	U2, U3, U6, U7	MAAM22010	MACOM	2.4-2.5 GHz LNA	MAAM22010
28	1	U4	UPG152TA	NEC	RF SWITCH	UPG152TA
29	5	U11, U12, U16, U18, U19	NC7S04M5	NATIONAL	INVERTER	NC7S04M5
30	1	U14	TKN11230B	TOKO	VOLTAGE REGULATOR	TK11230B
31	1	U17	RF2128P	RFMD	MEDIUM POWER LINEAR AMPLIFIER	RF2128P
32	1				BOARD	B500.641.024 VOL.

FIG. 66B

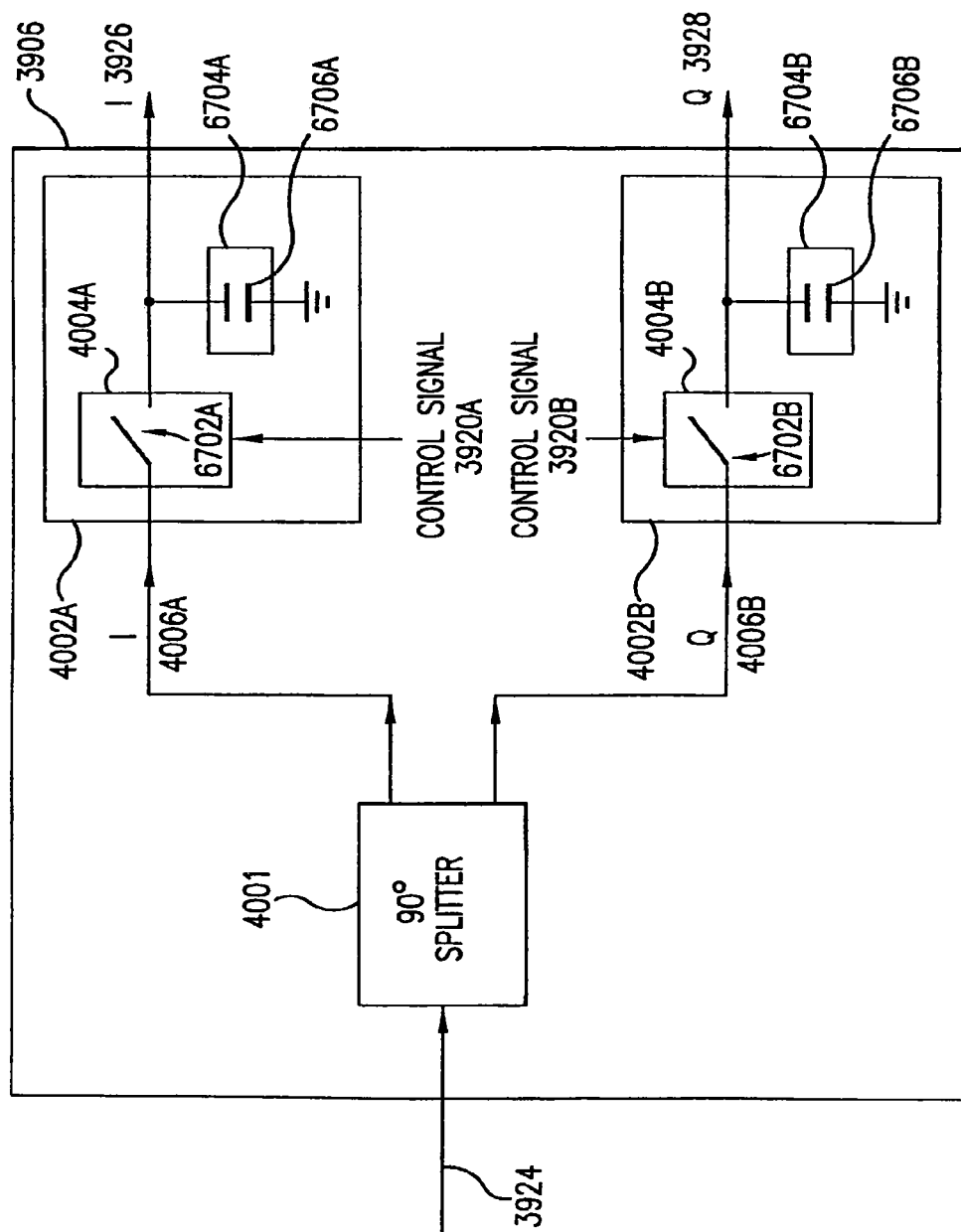


FIG. 67A

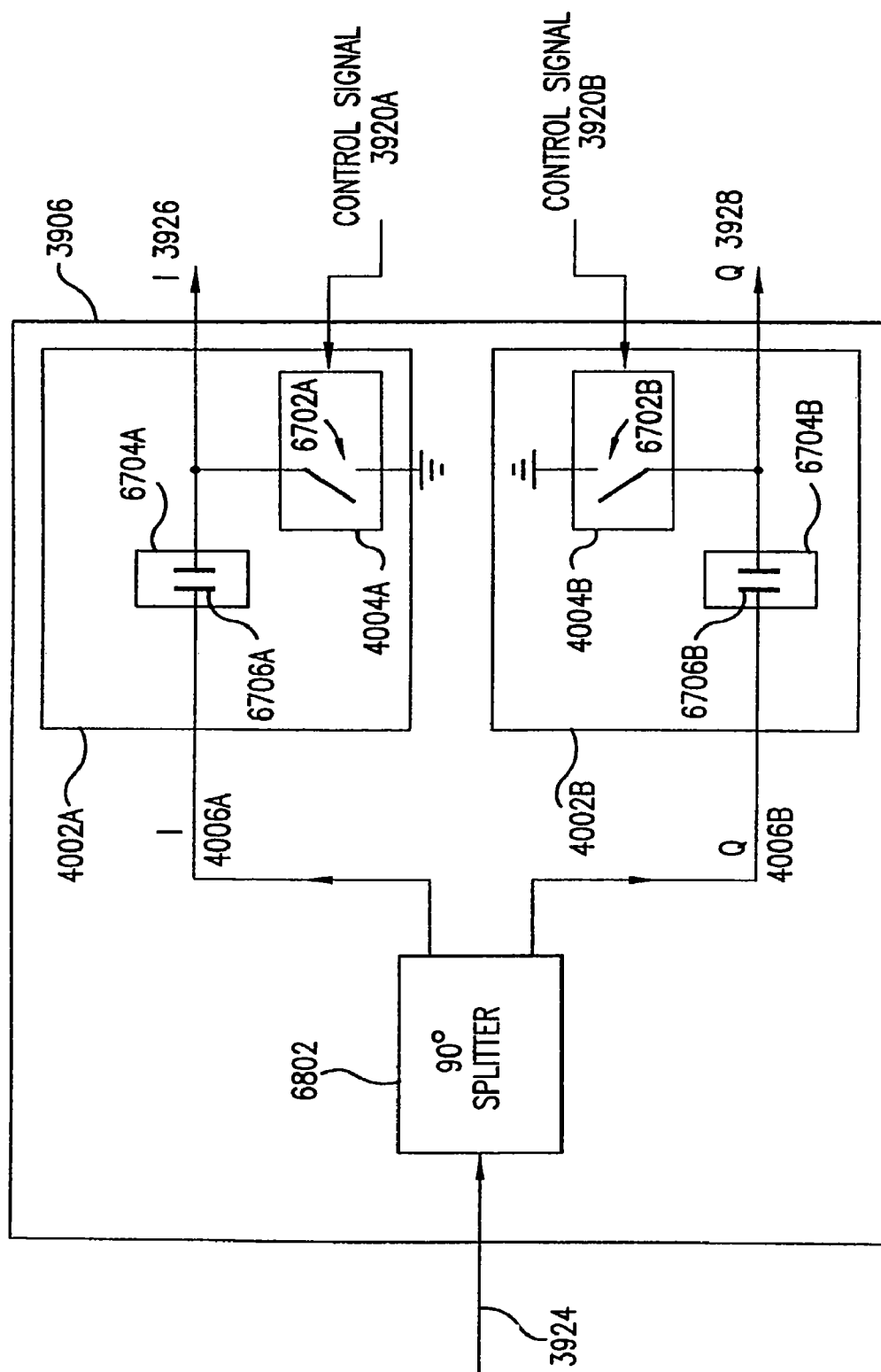


FIG. 67B



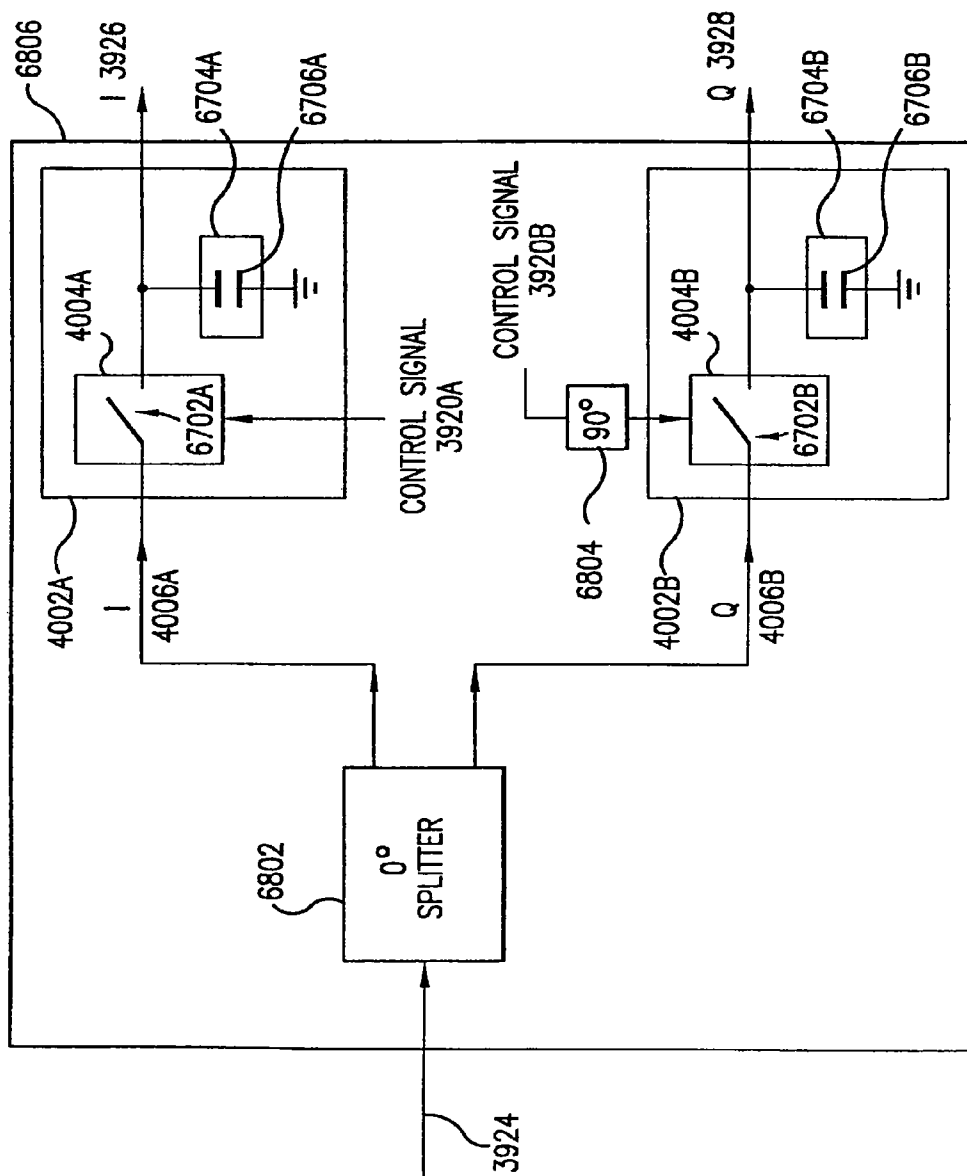


FIG. 68A

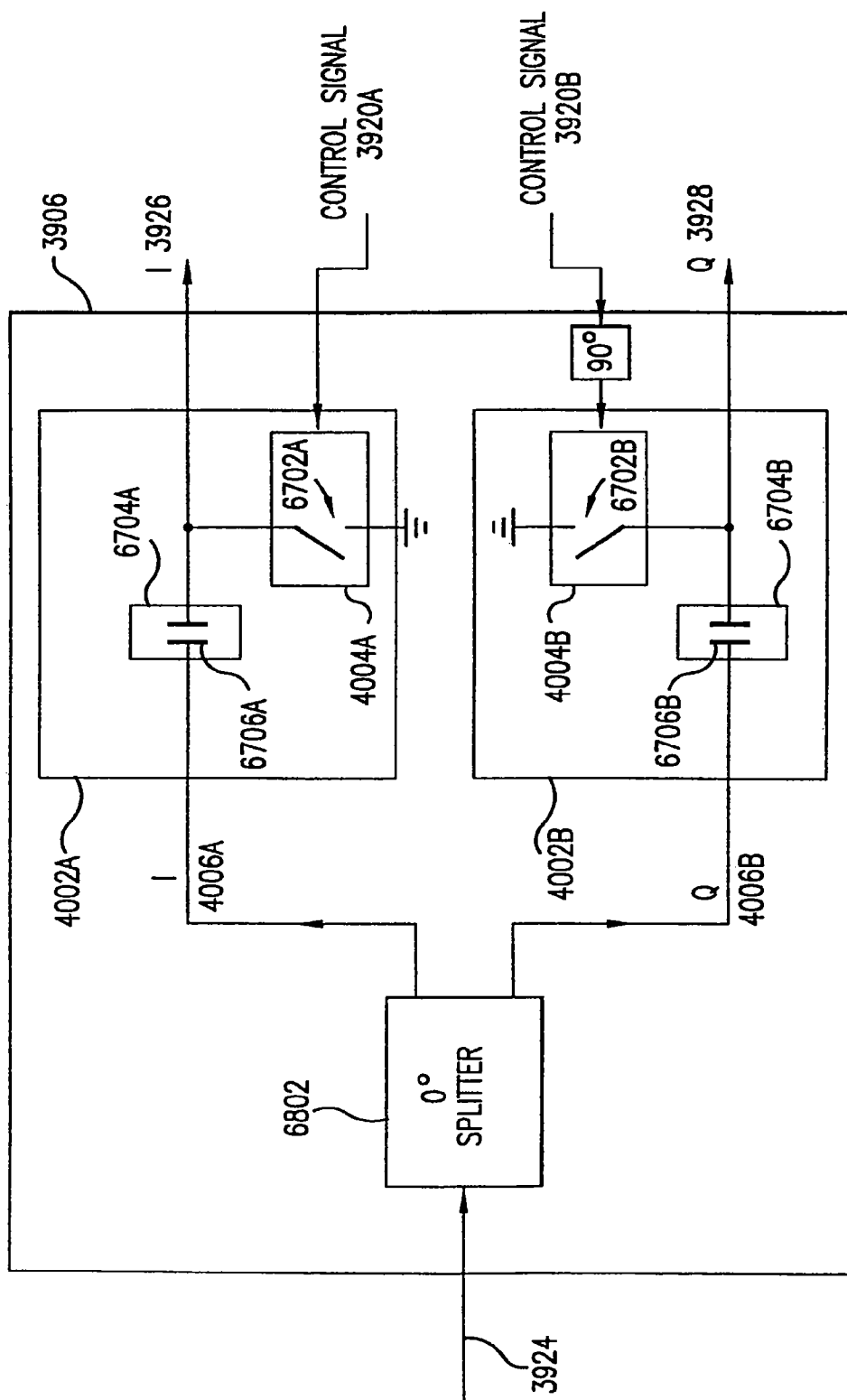


FIG. 68B

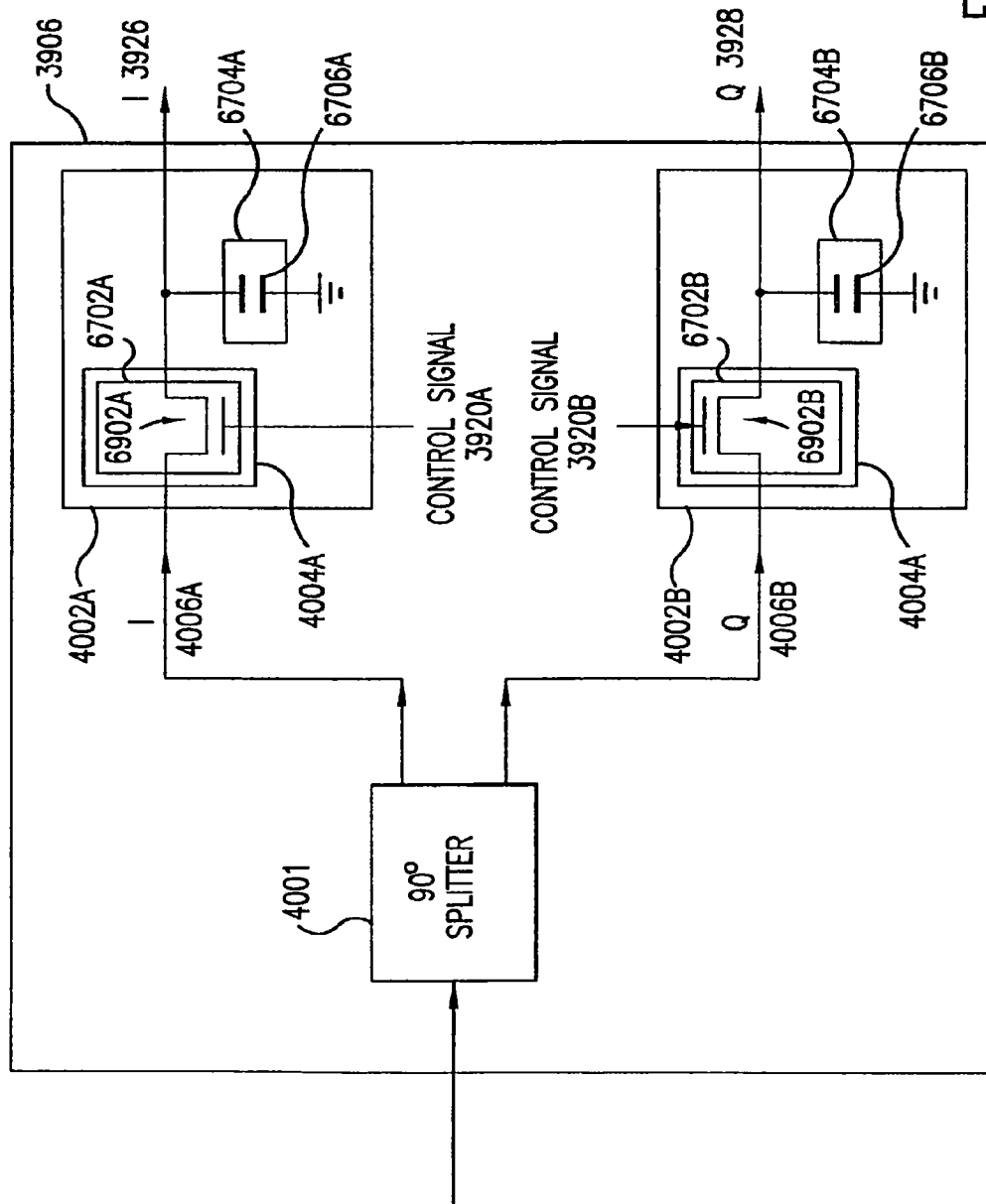


FIG. 69A

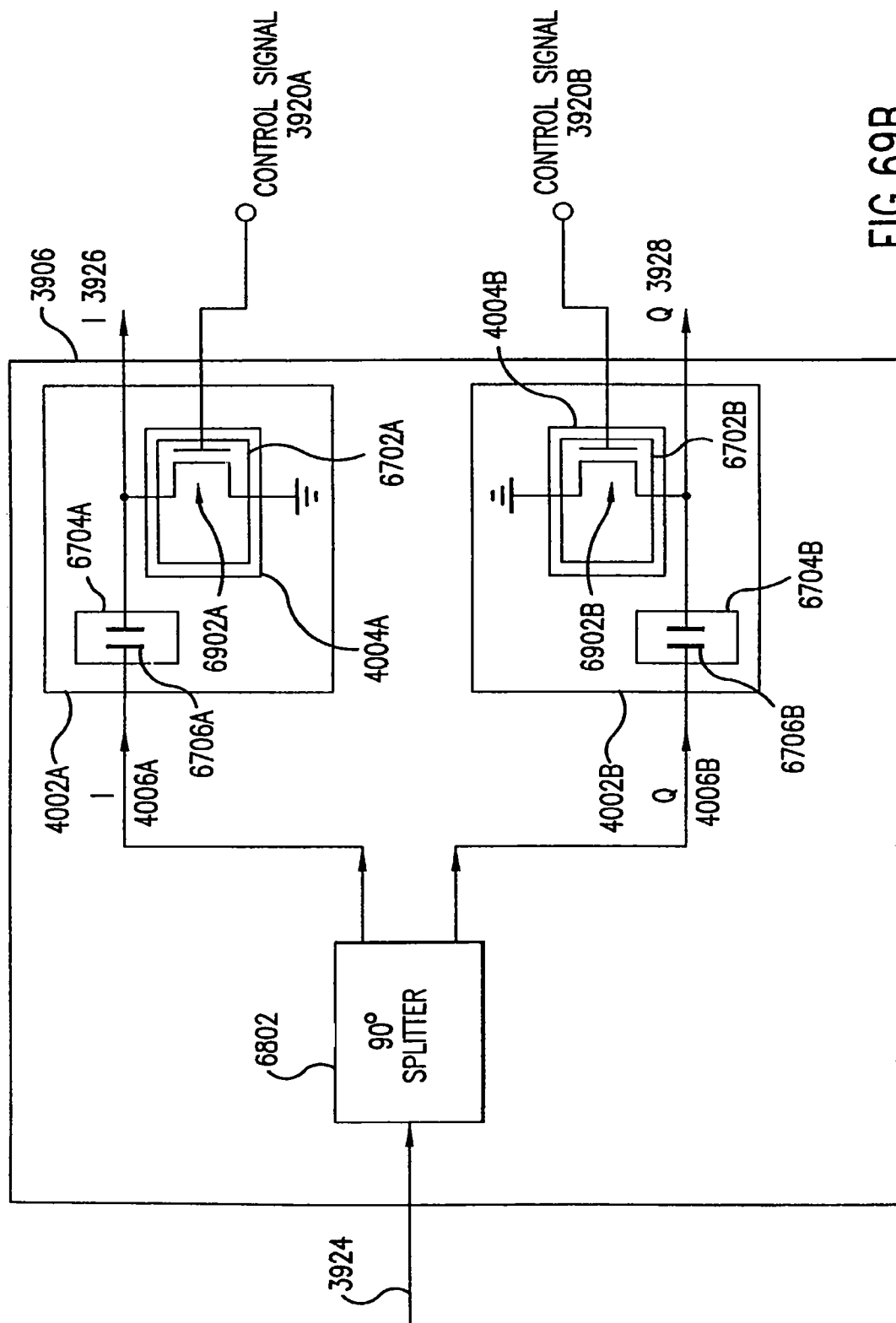


FIG. 69B

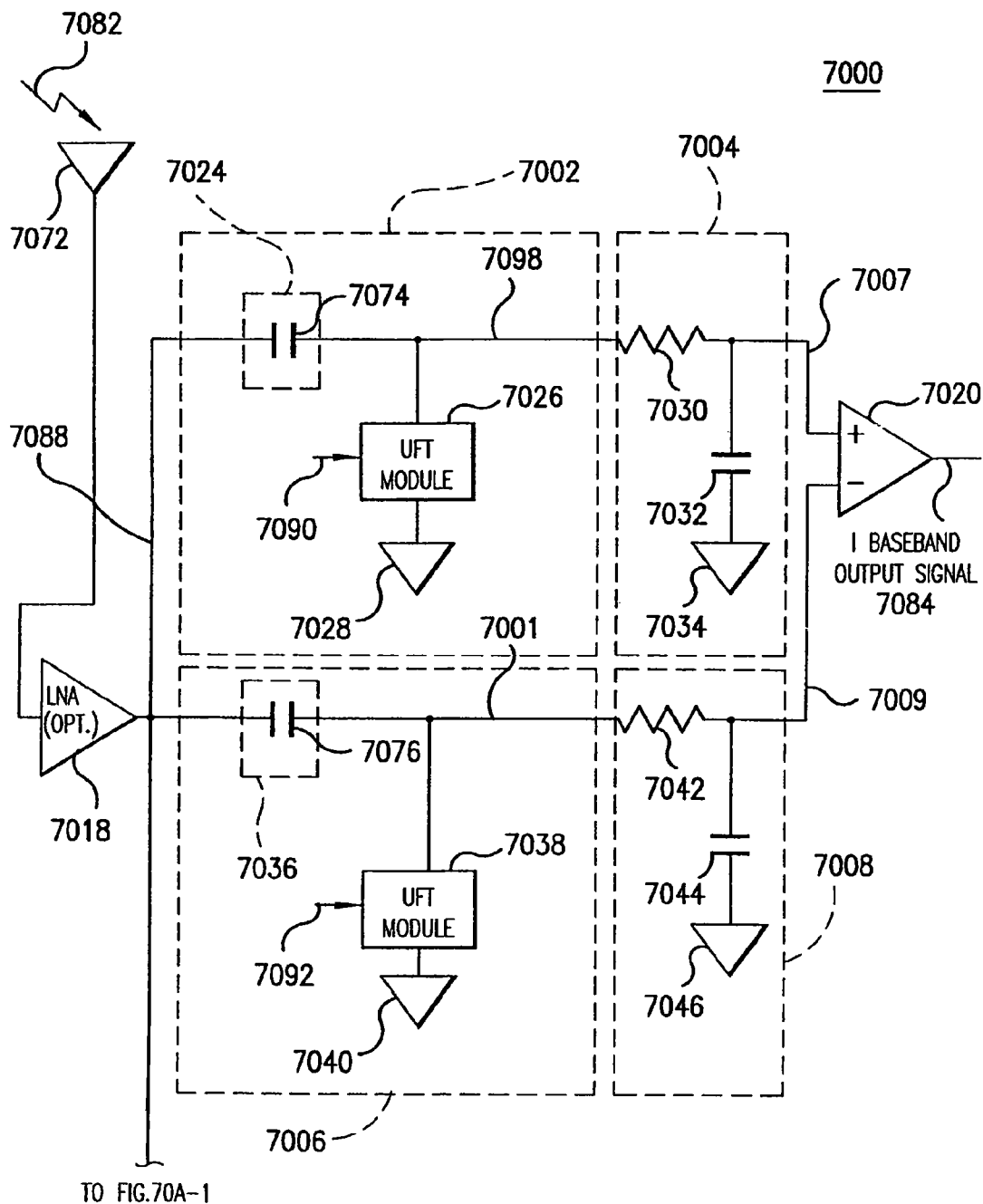


FIG. 70A

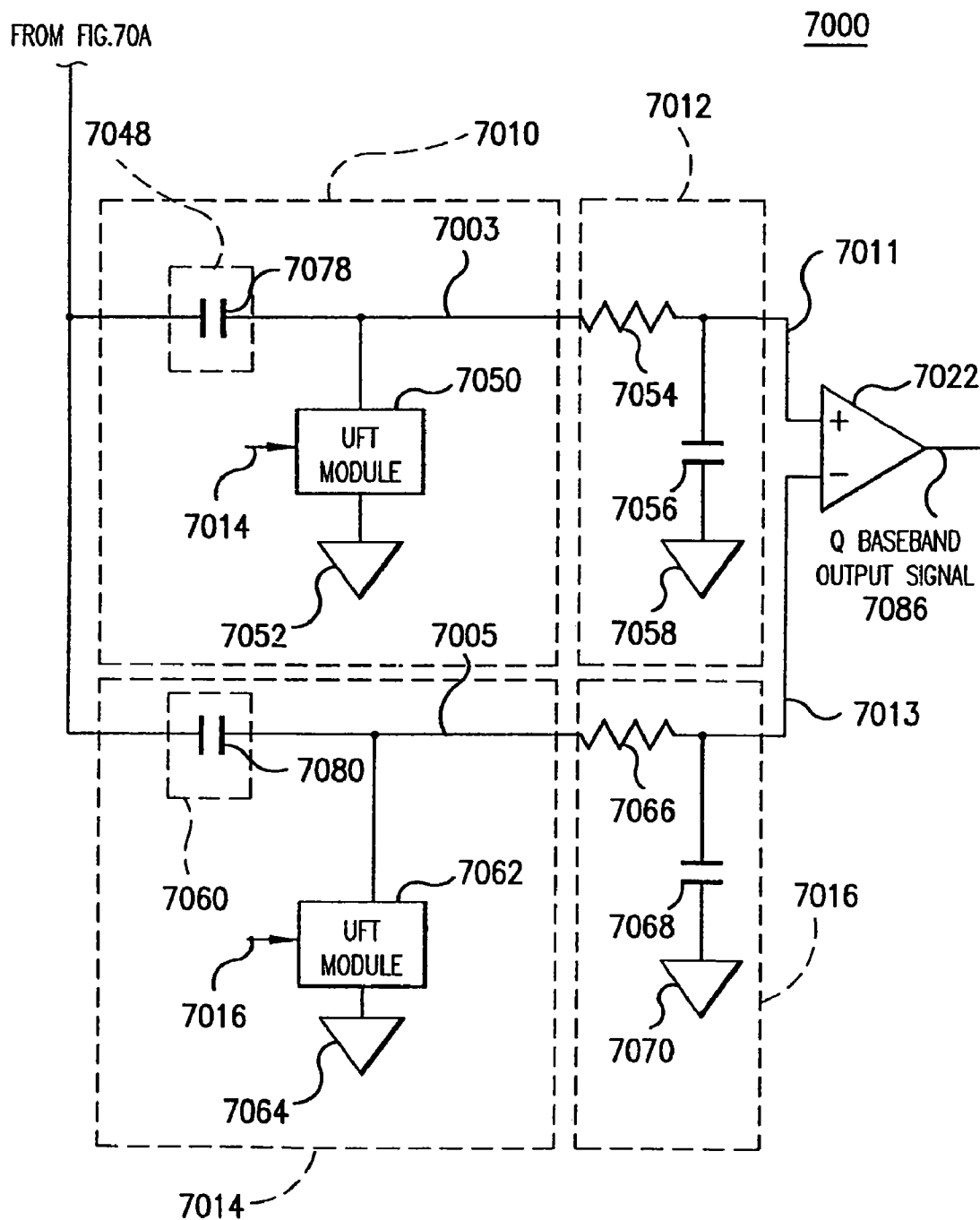


FIG. 70A-1

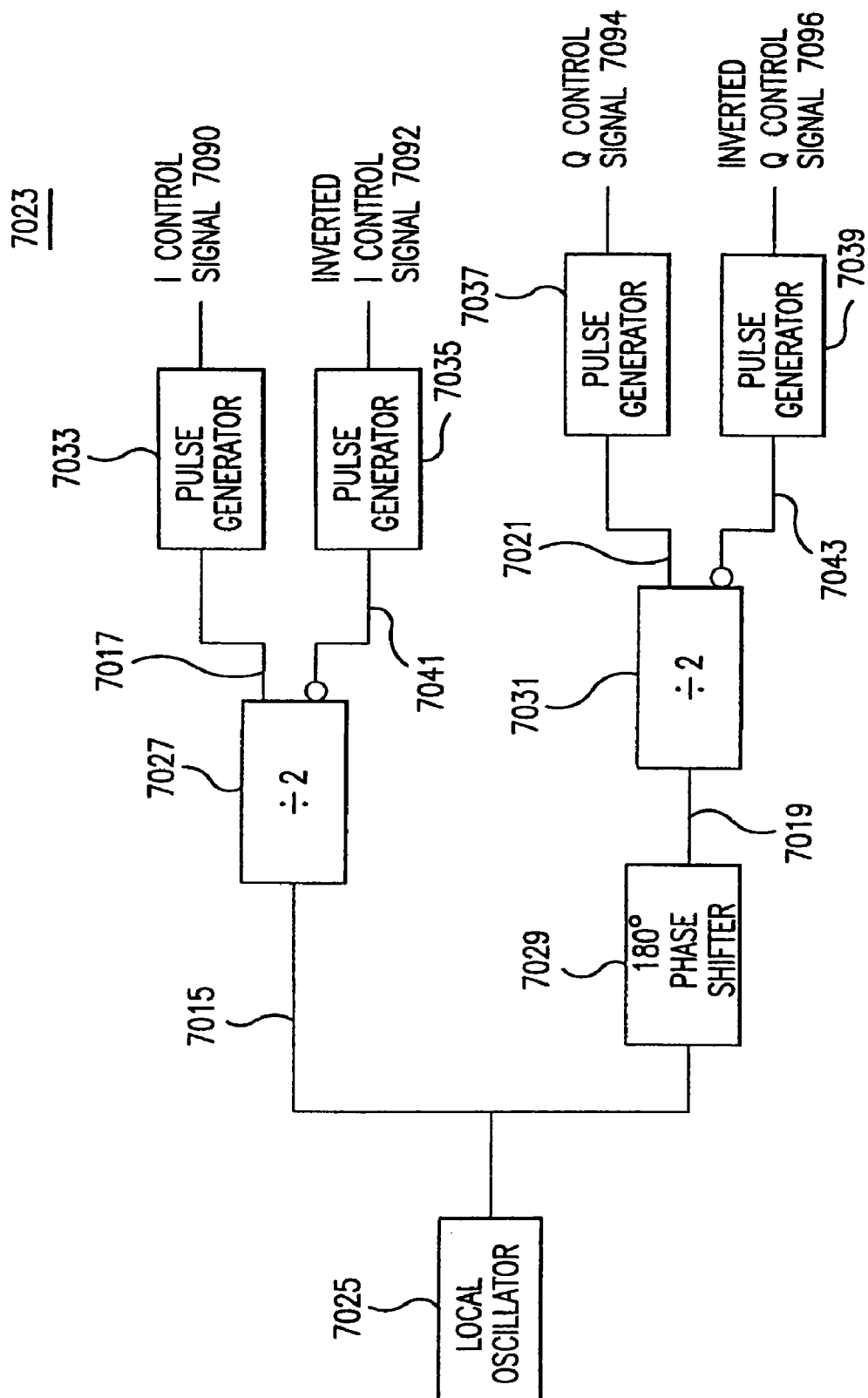


FIG. 70B

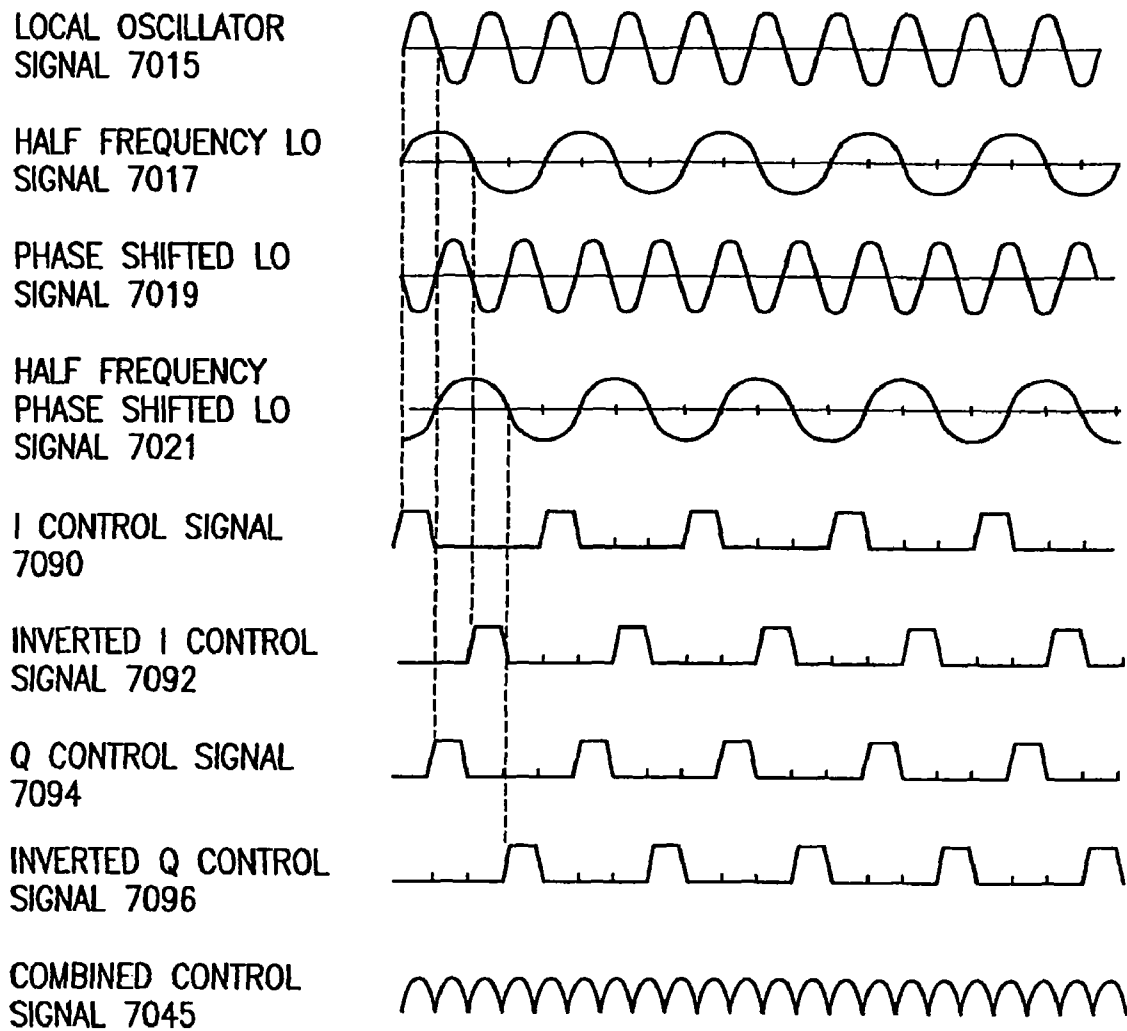


FIG.70C



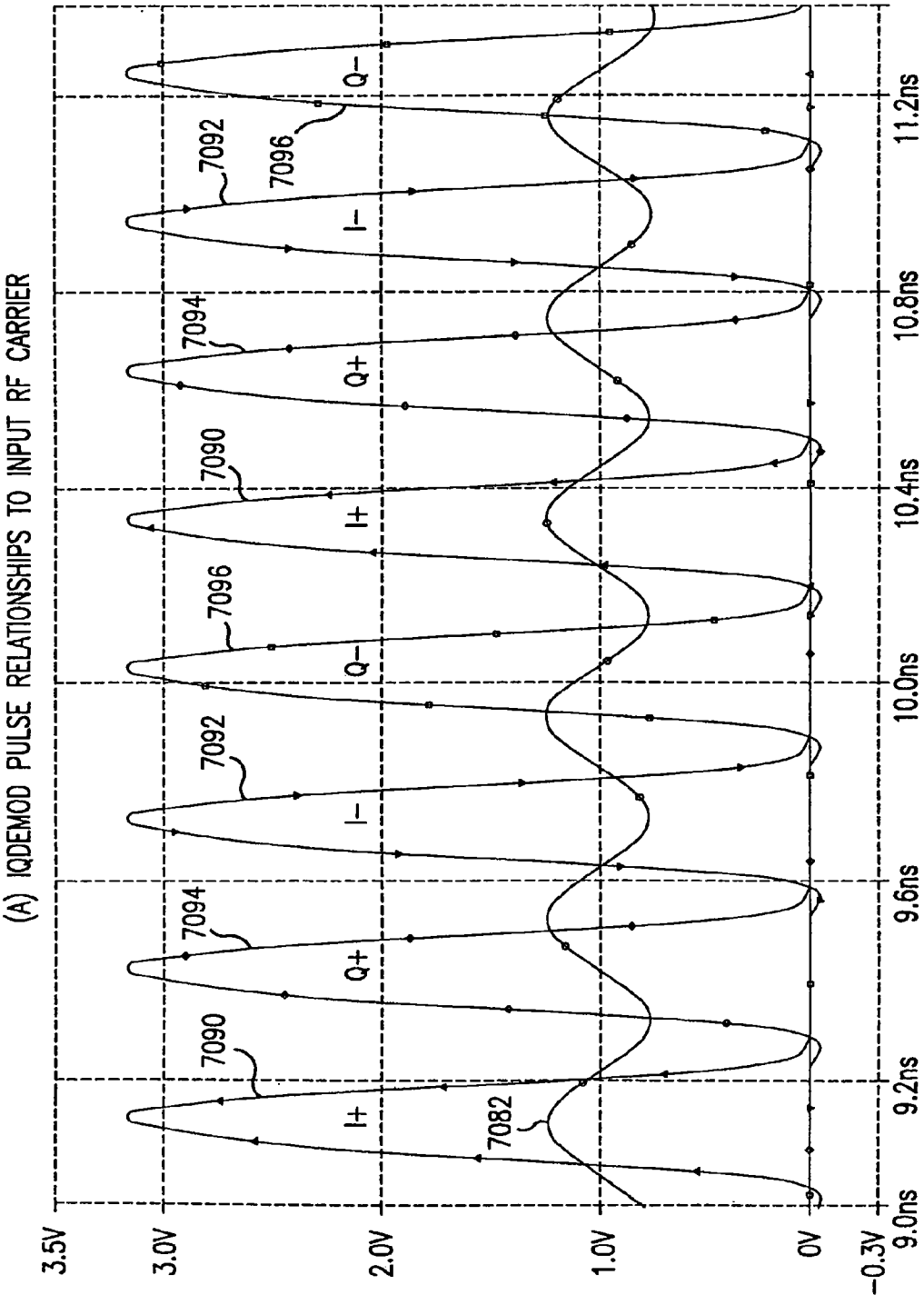
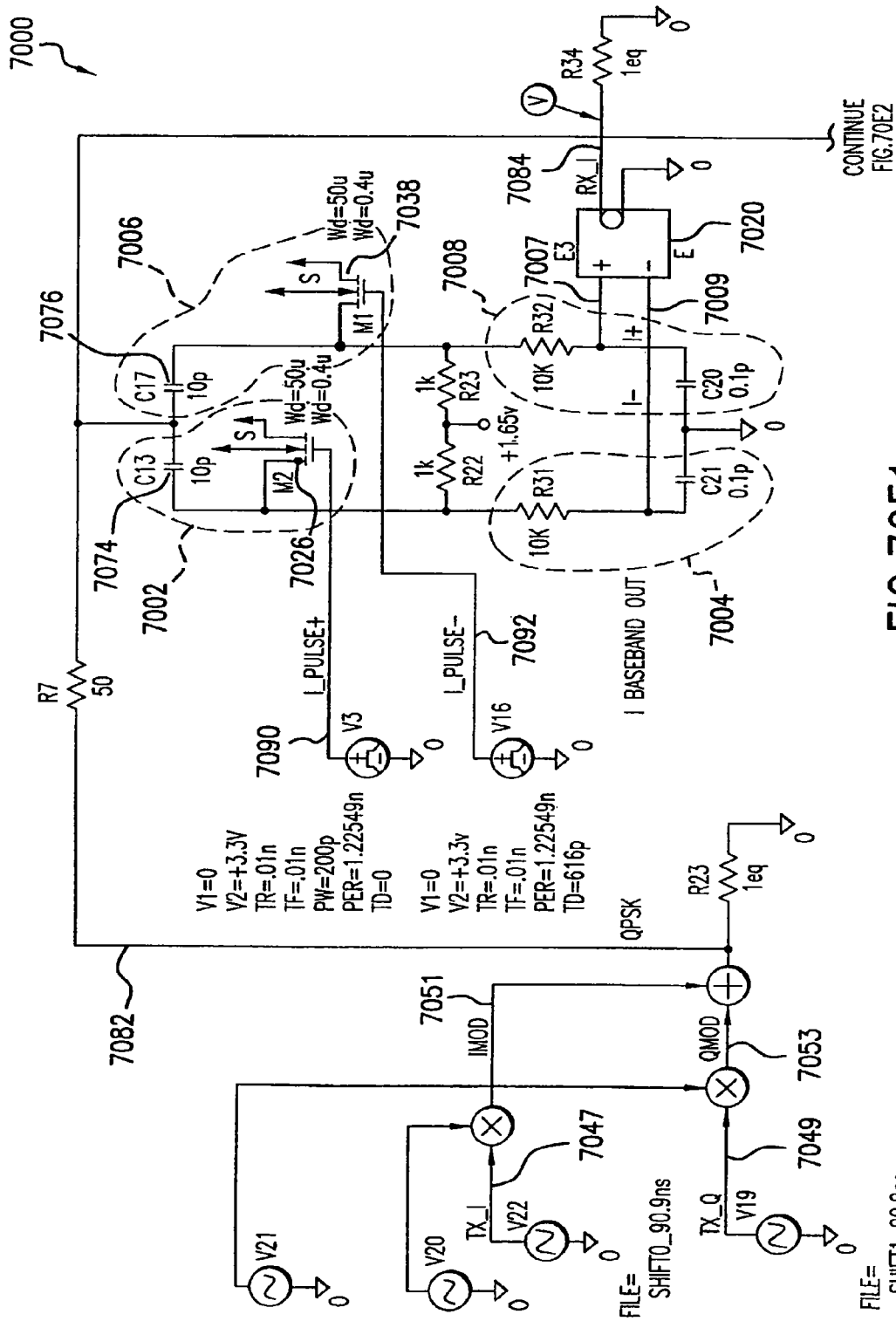
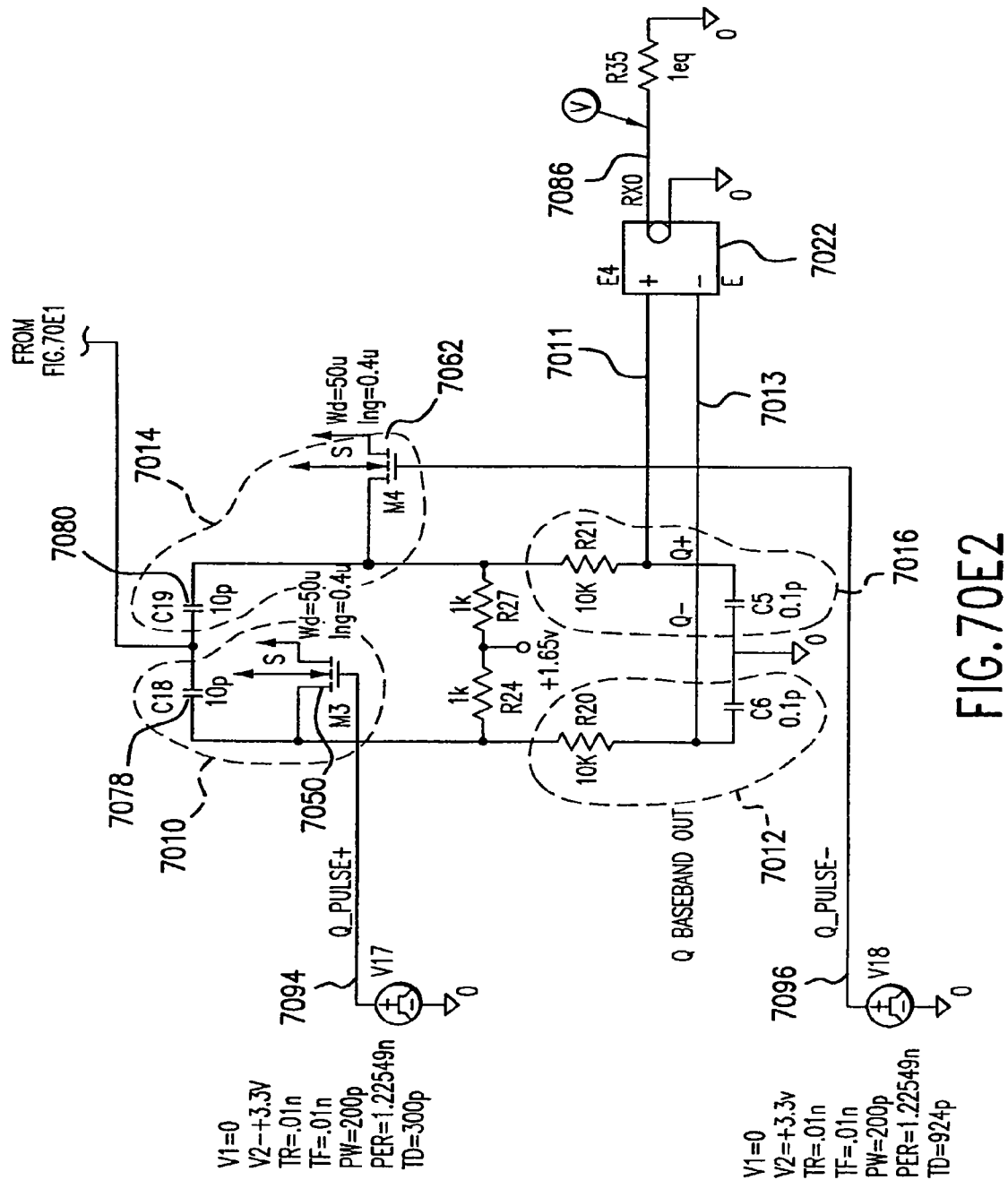


FIG.70D





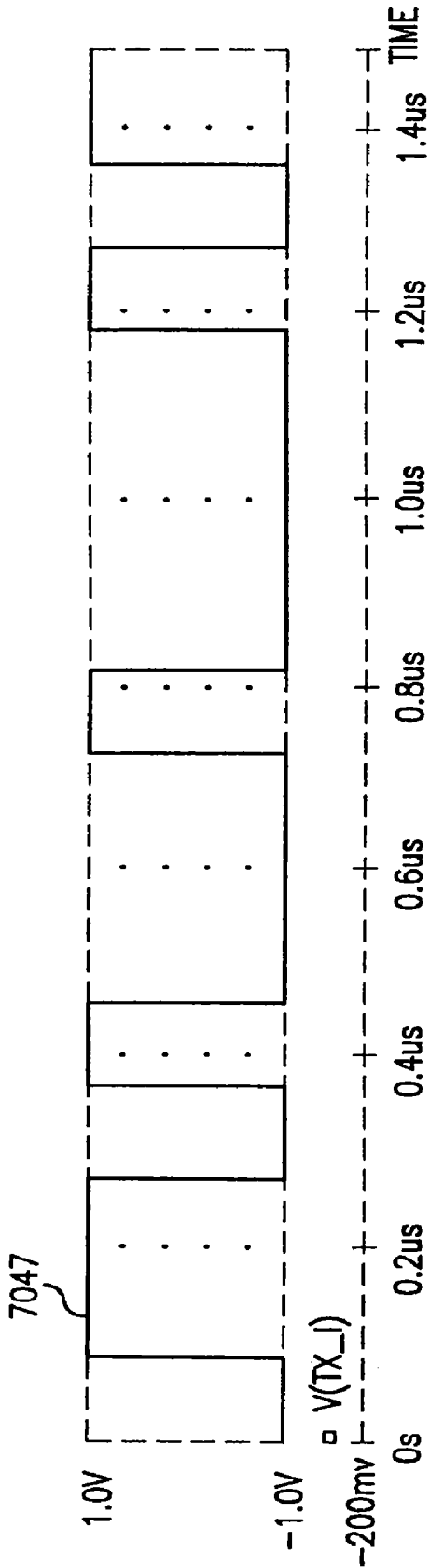


FIG.70F

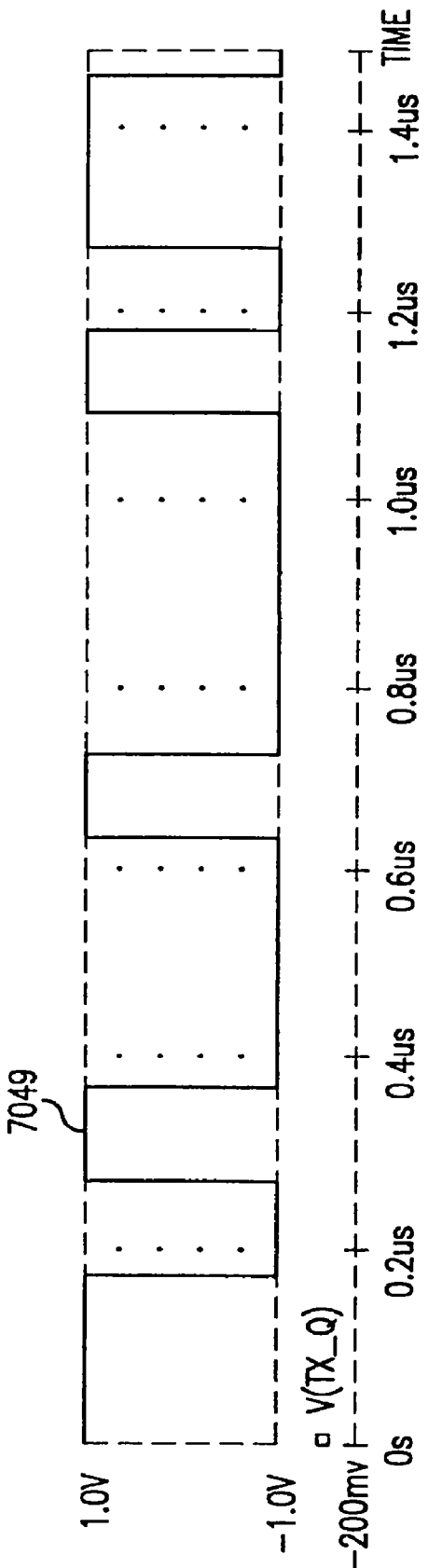


FIG.70G

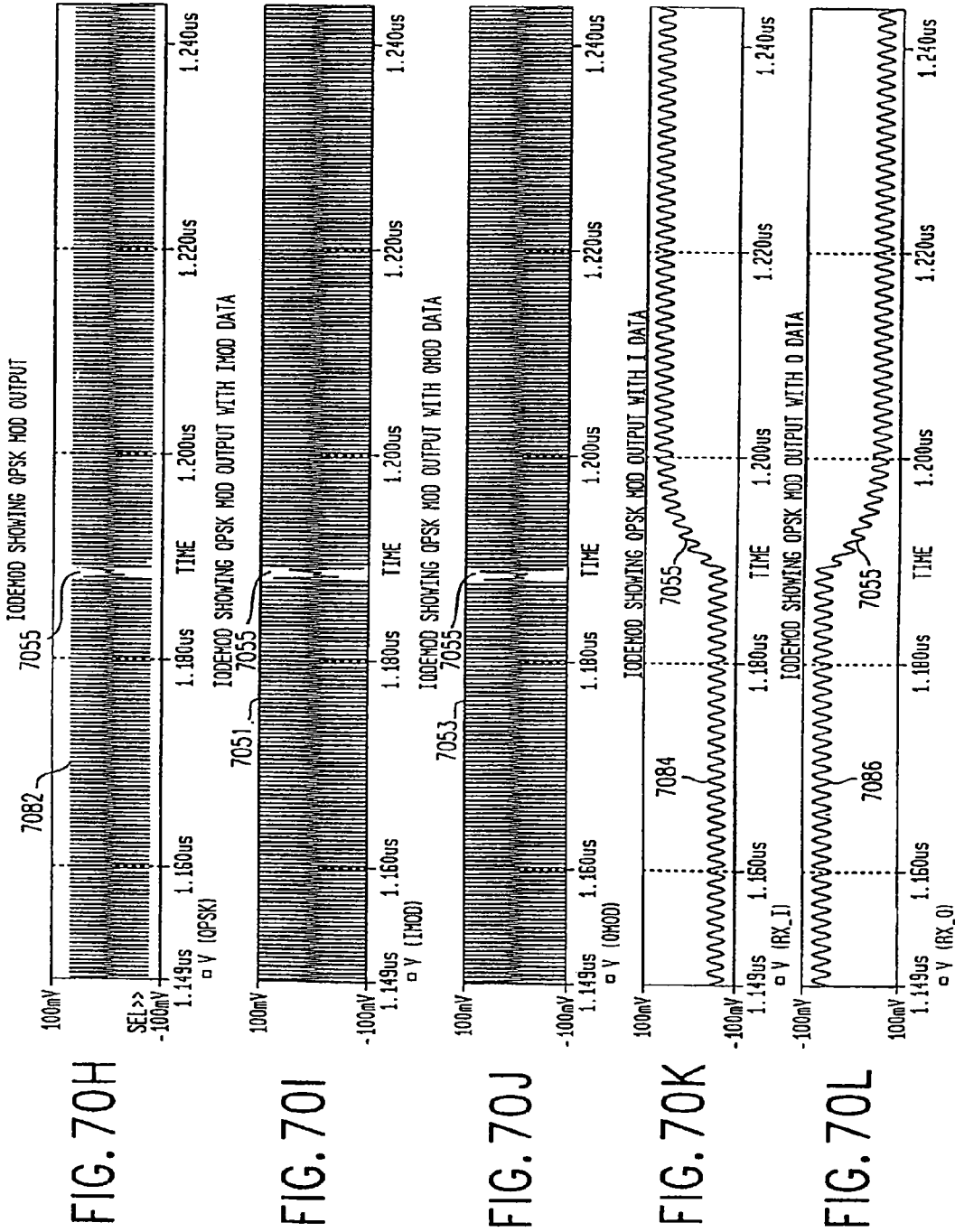


FIG. 70M

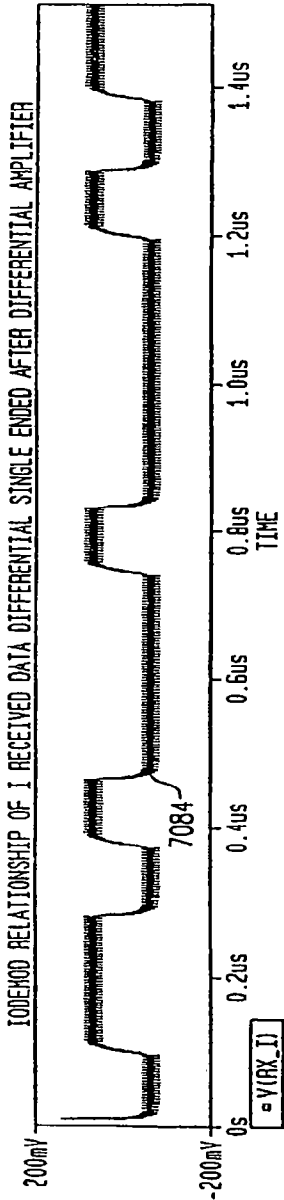


FIG. 70N

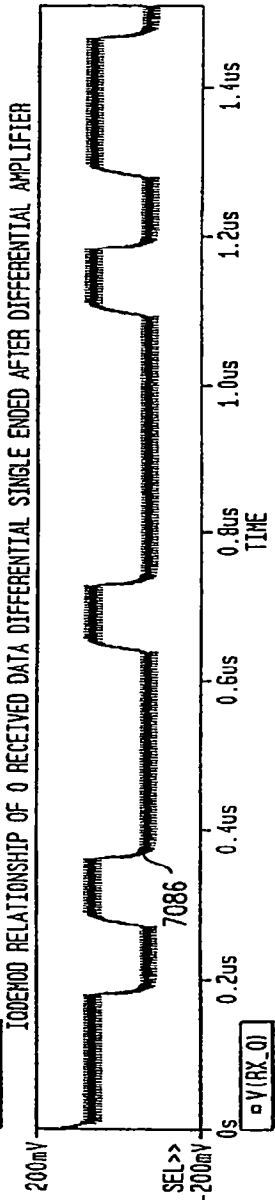


FIG. 70O

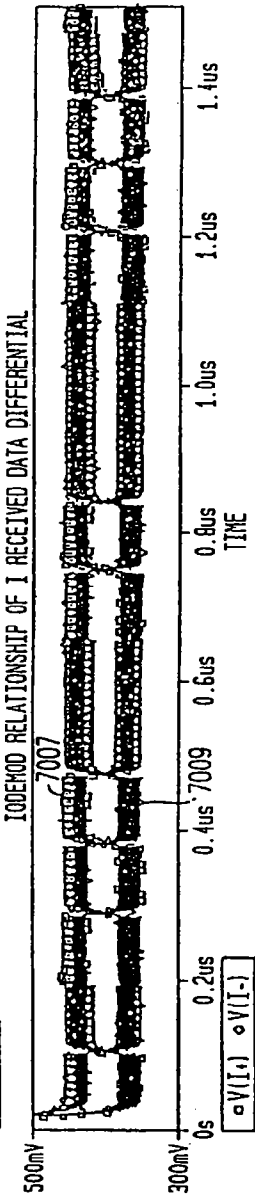
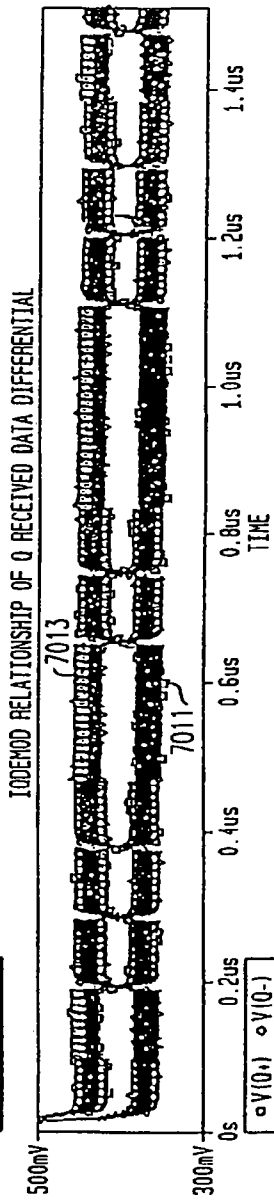


FIG. 70P



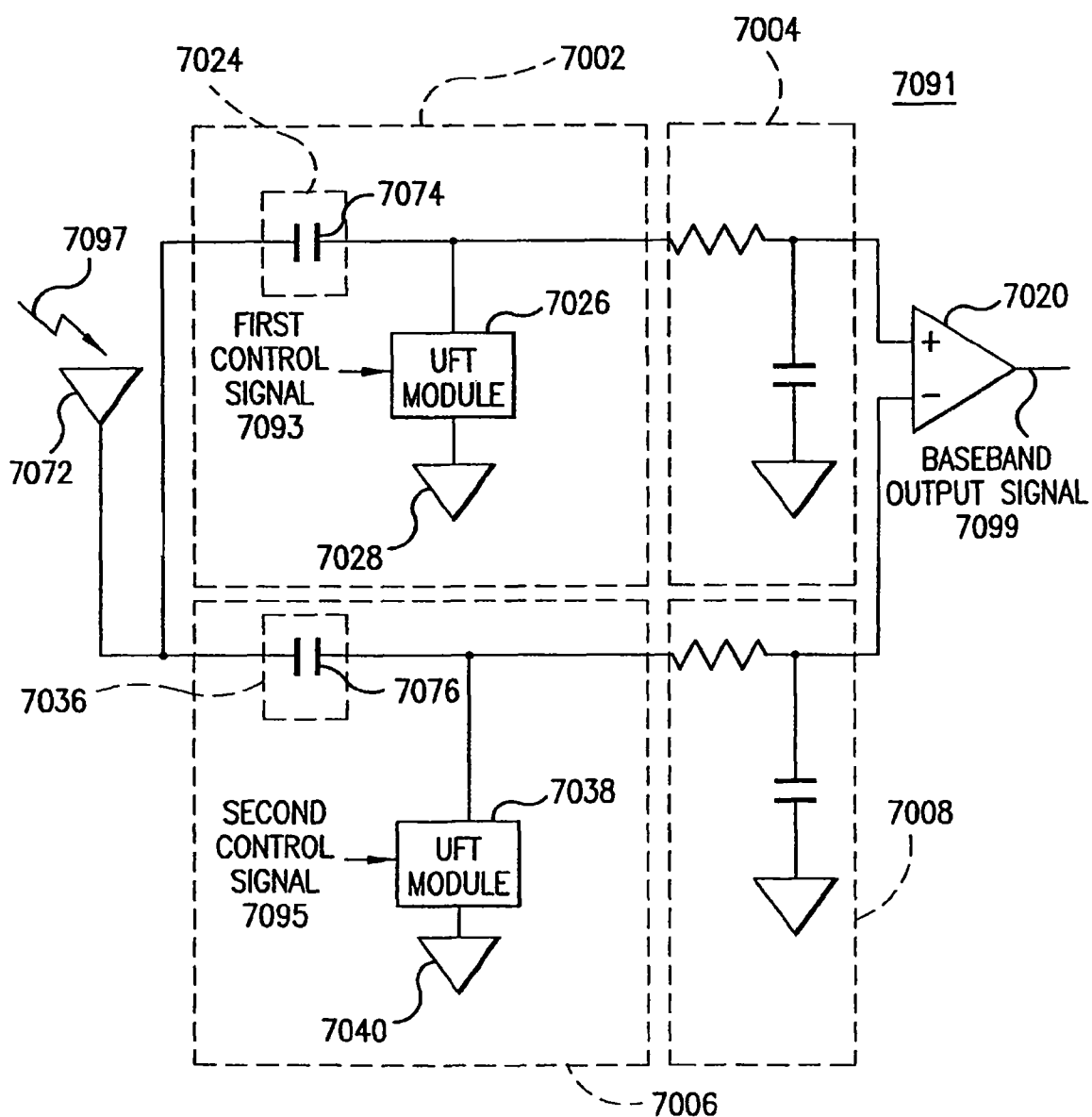


FIG. 700Q

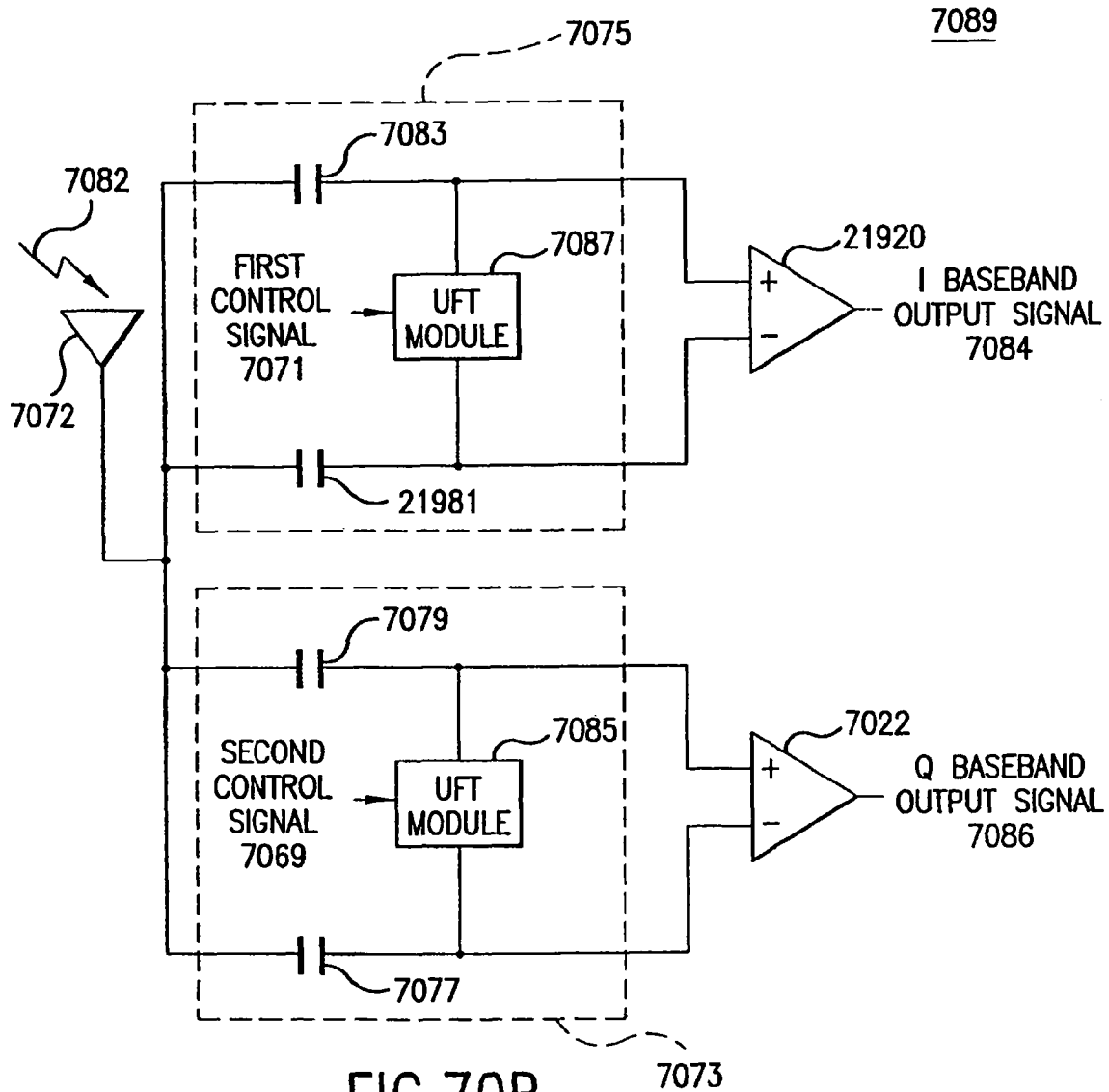
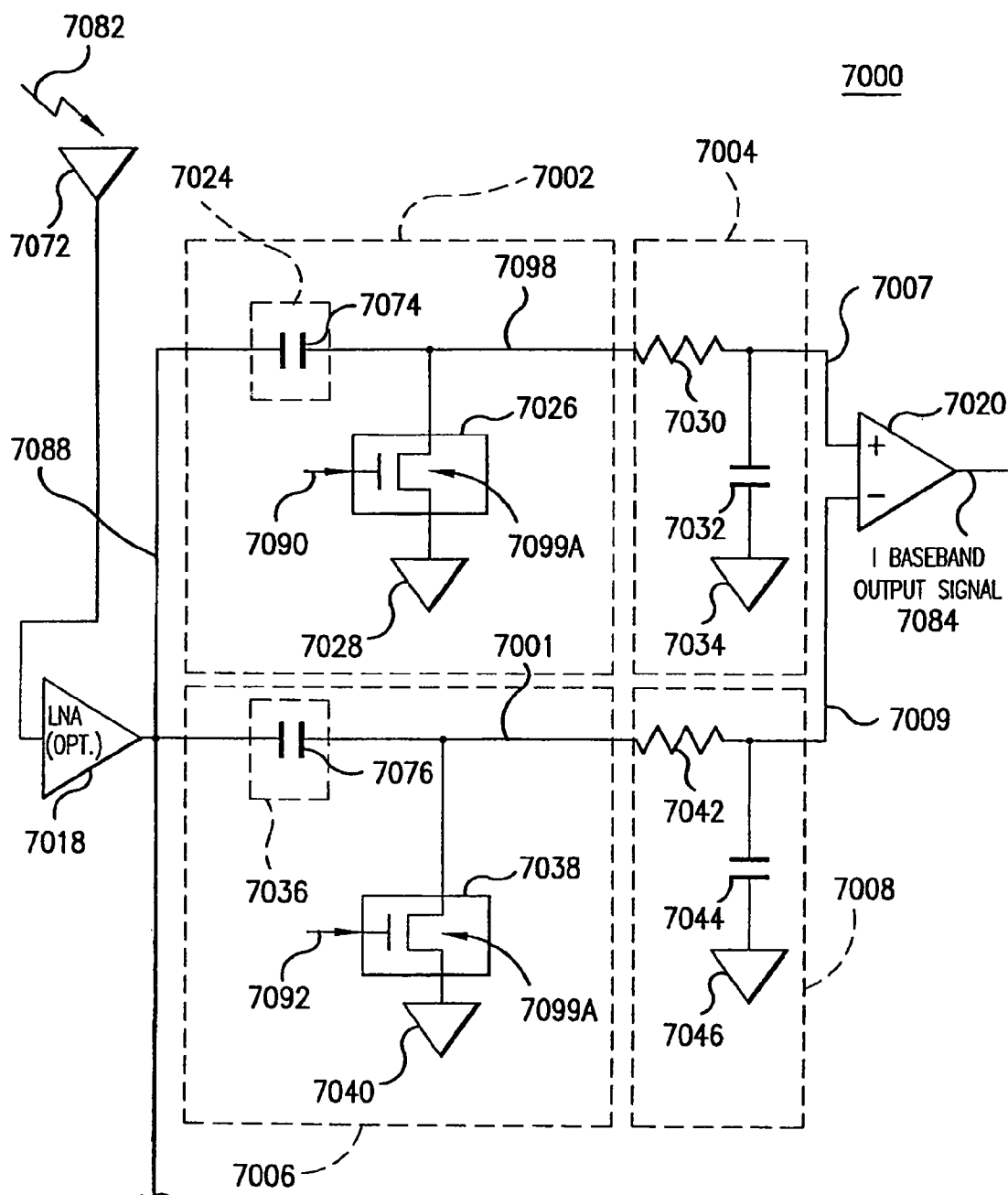


FIG. 70R





TO FIG.70S-1

FIG.70S

FROM FIG. 70S

7000

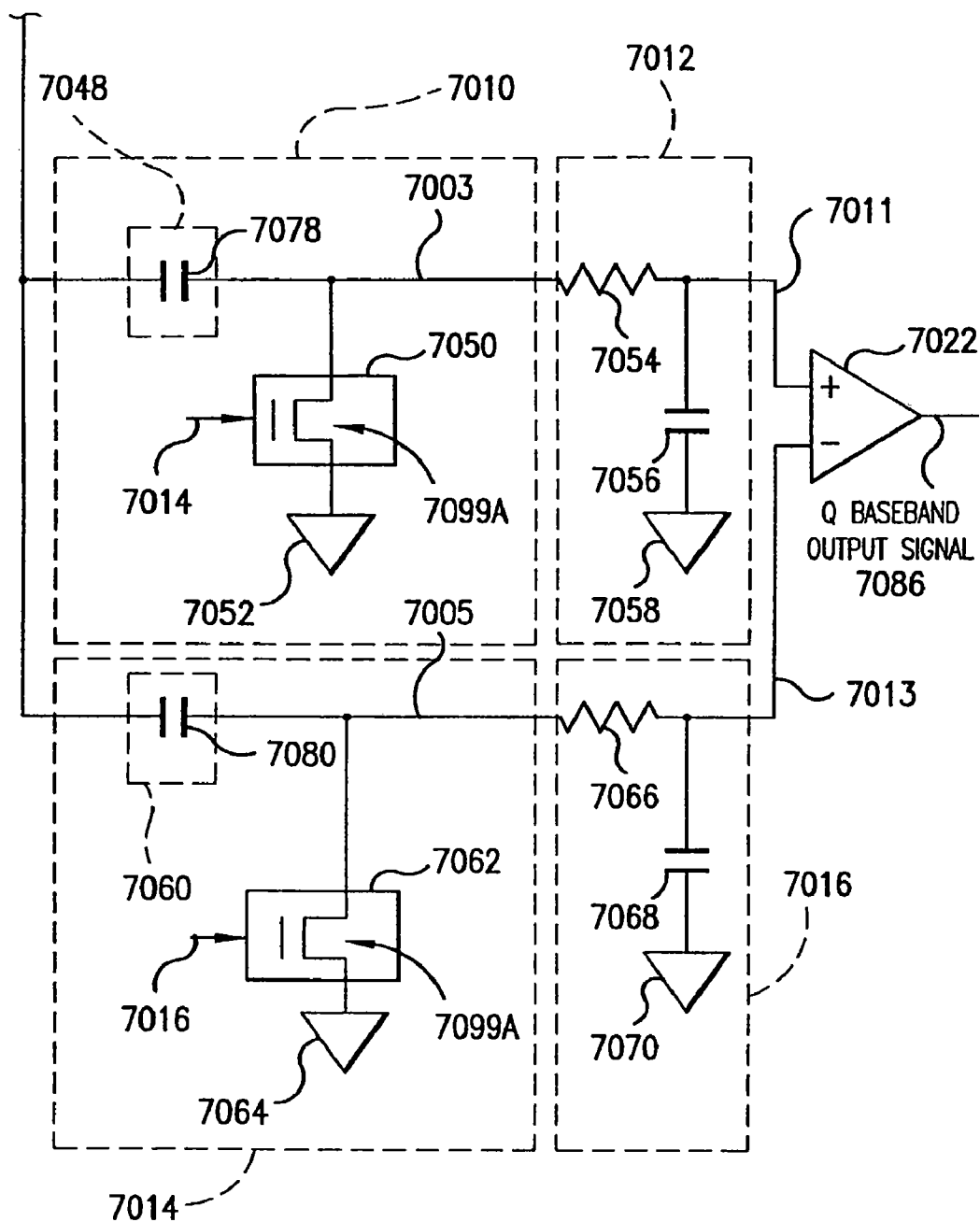


FIG. 70S-1

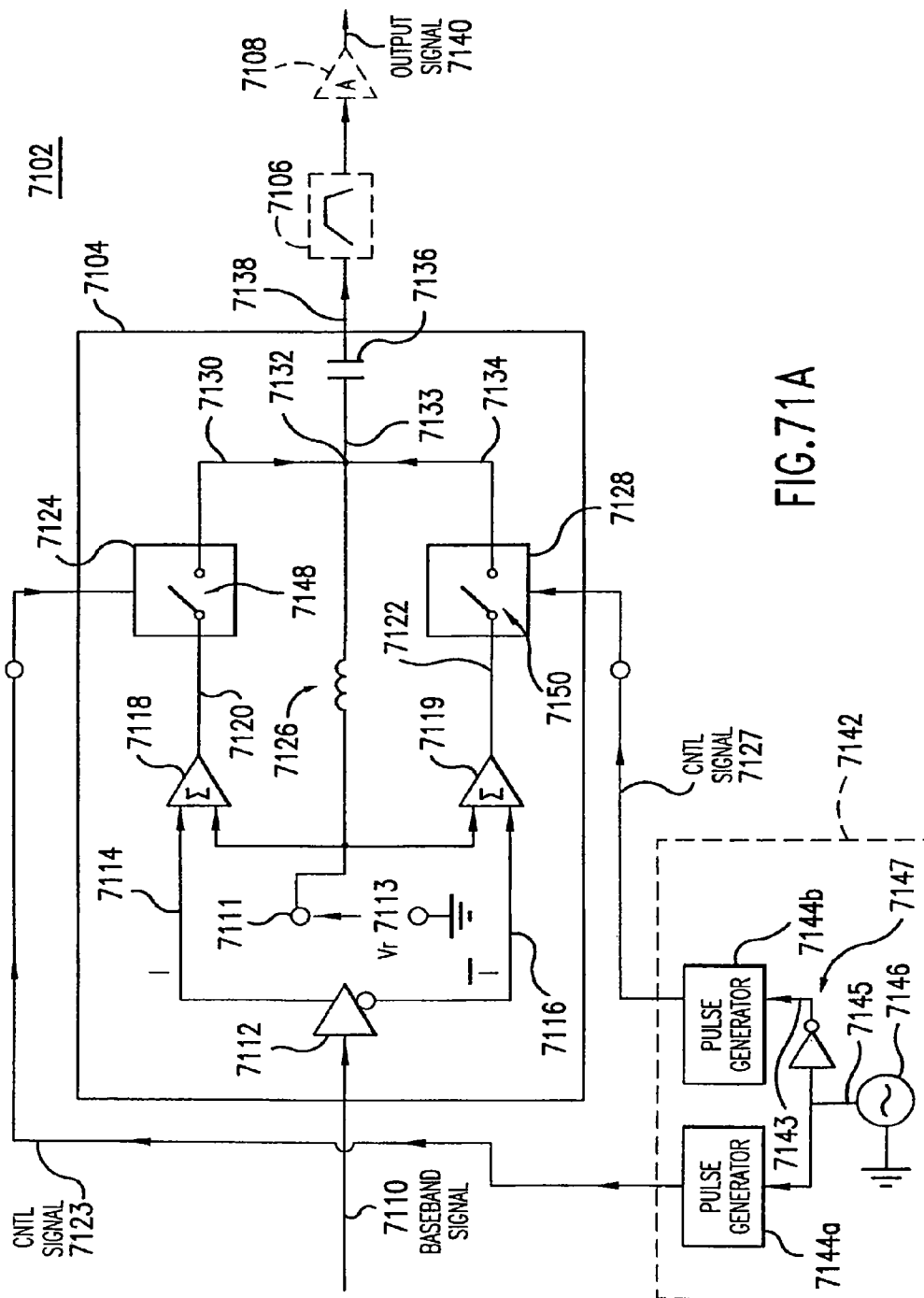
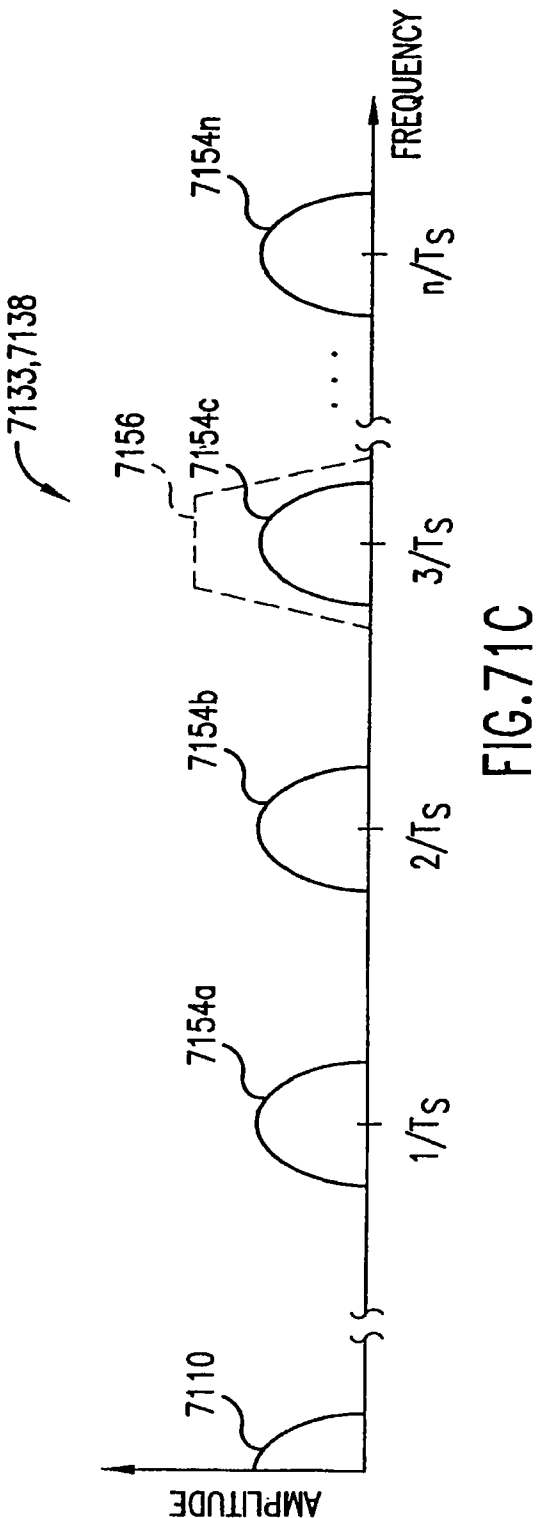
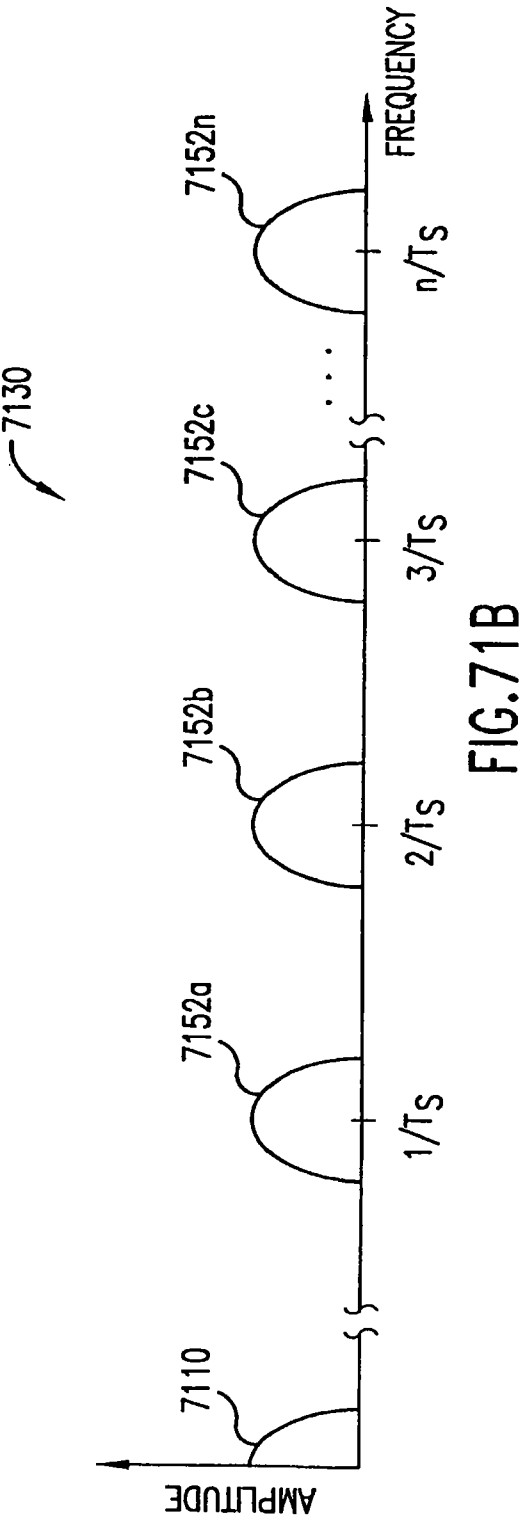
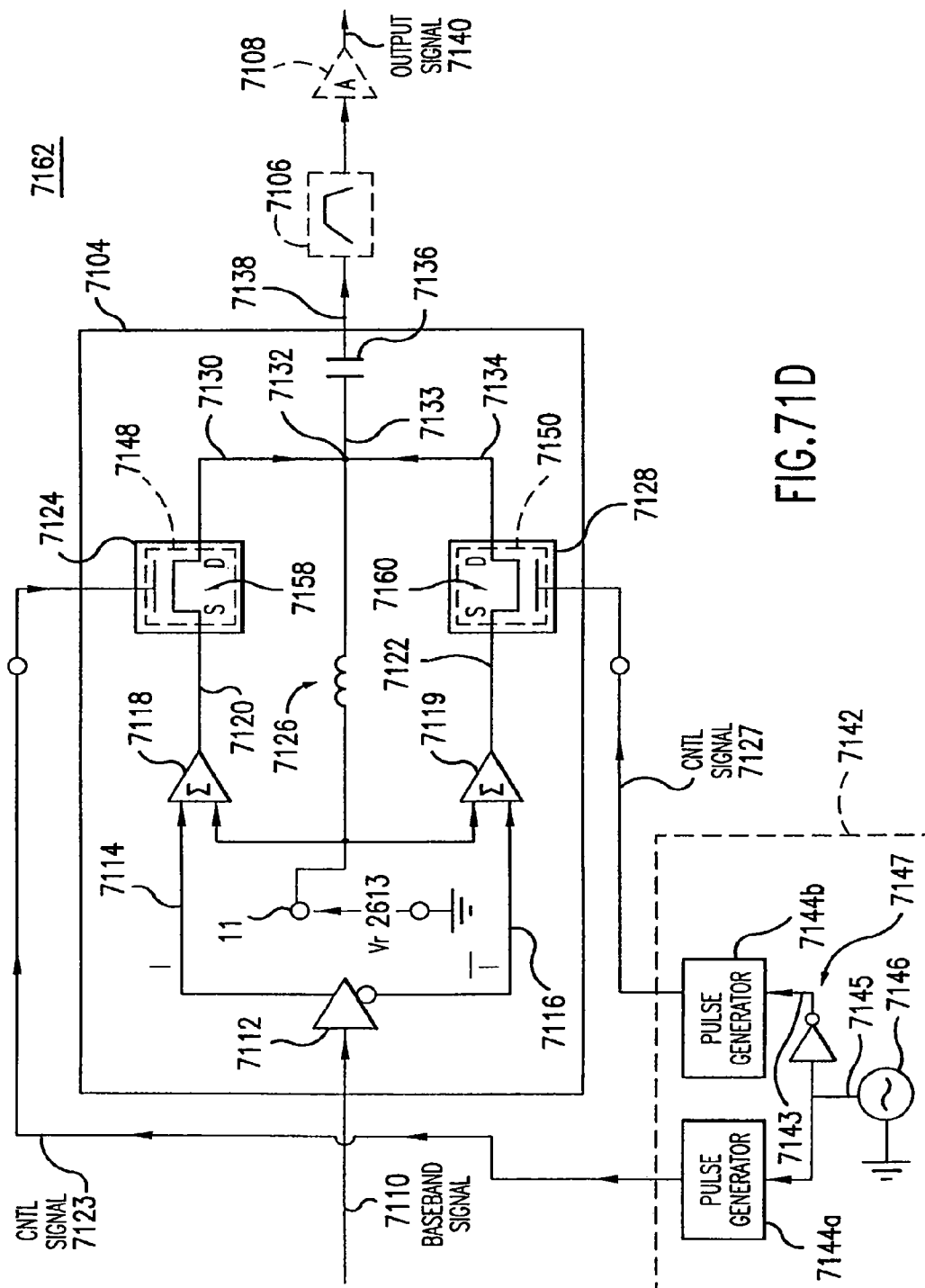


FIG. 711A





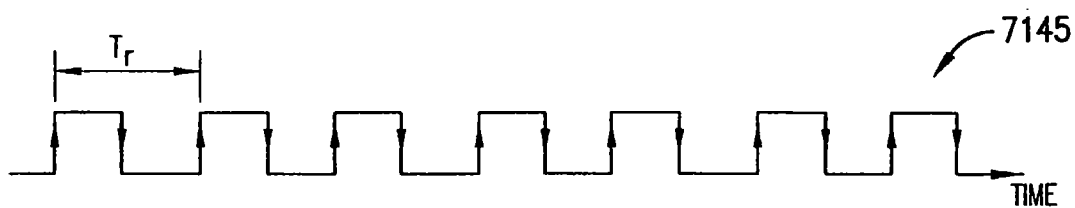


FIG.72A

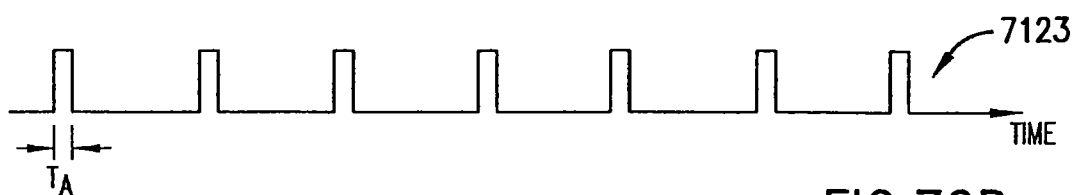


FIG.72B

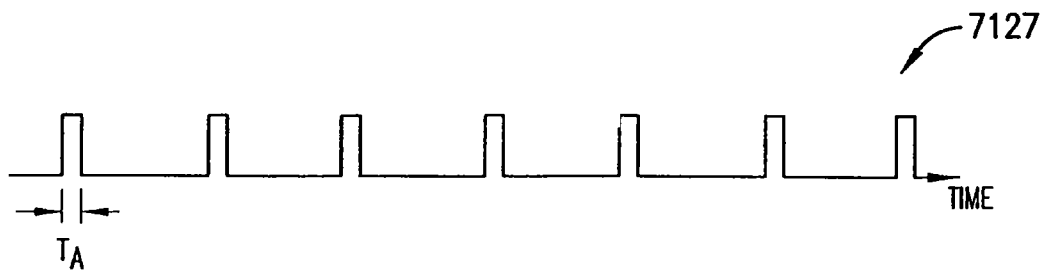


FIG.72C

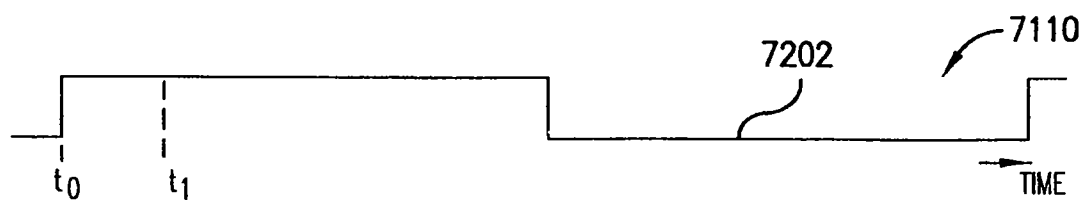


FIG.72D

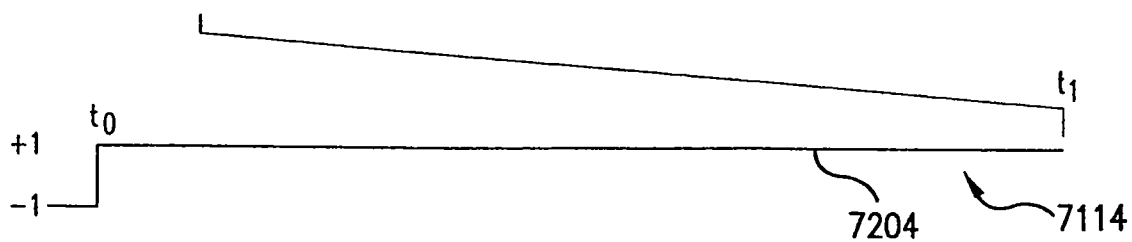


FIG.72E

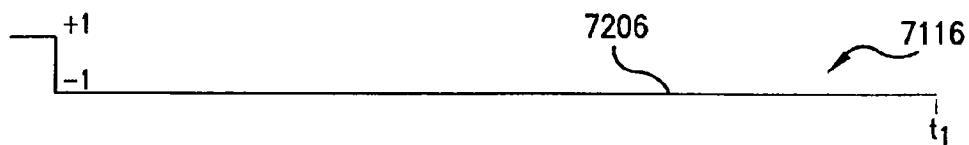


FIG. 72F



FIG. 72G

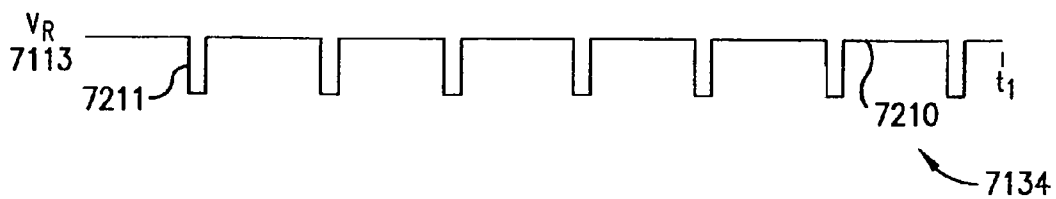


FIG. 72H

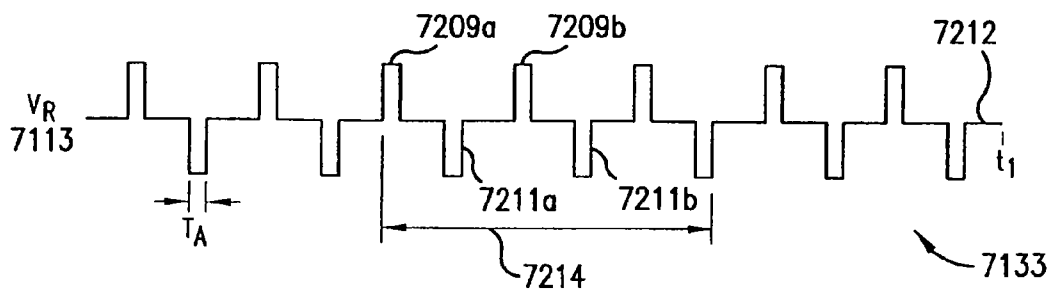


FIG. 72I

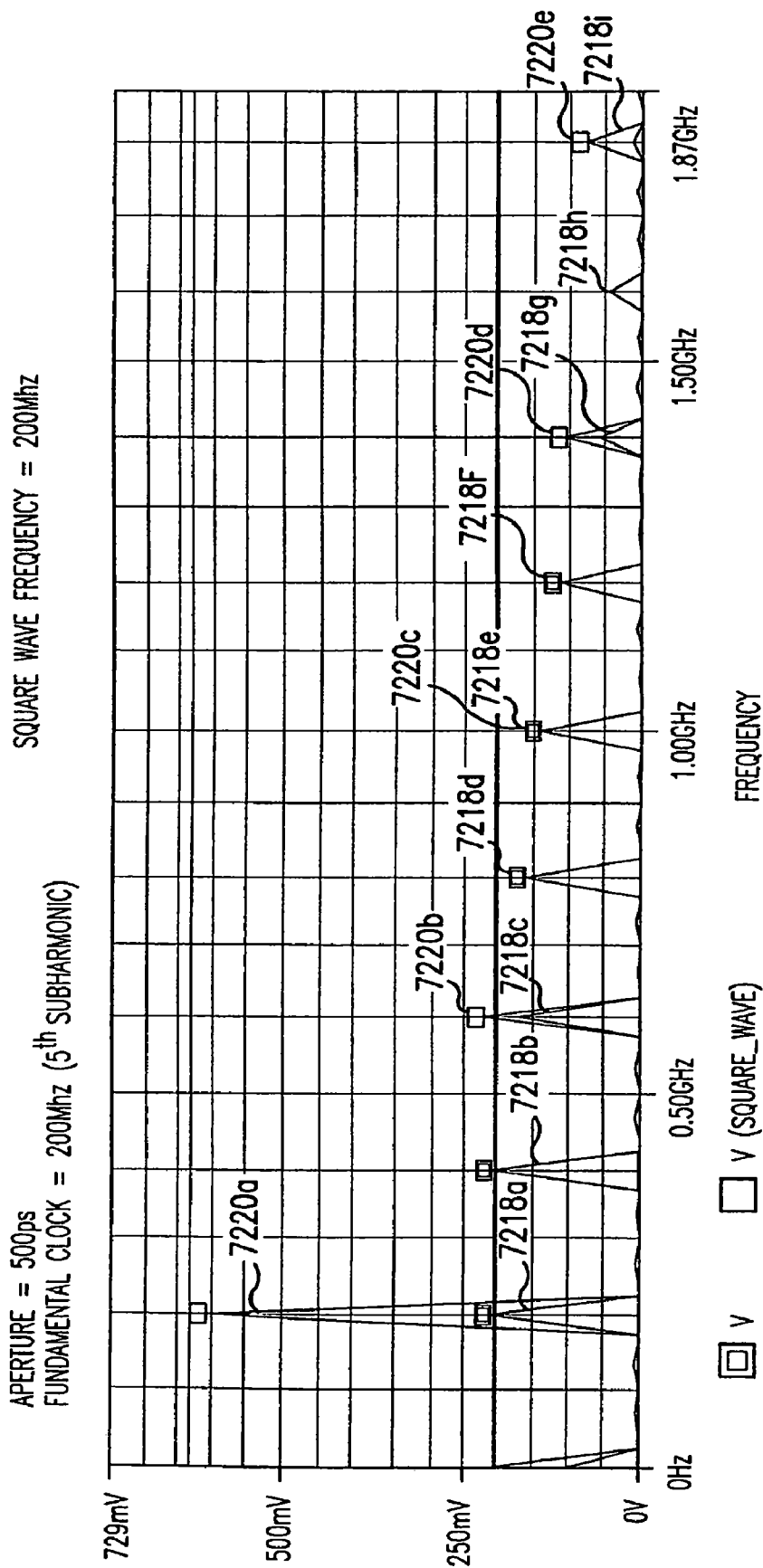


FIG.72J



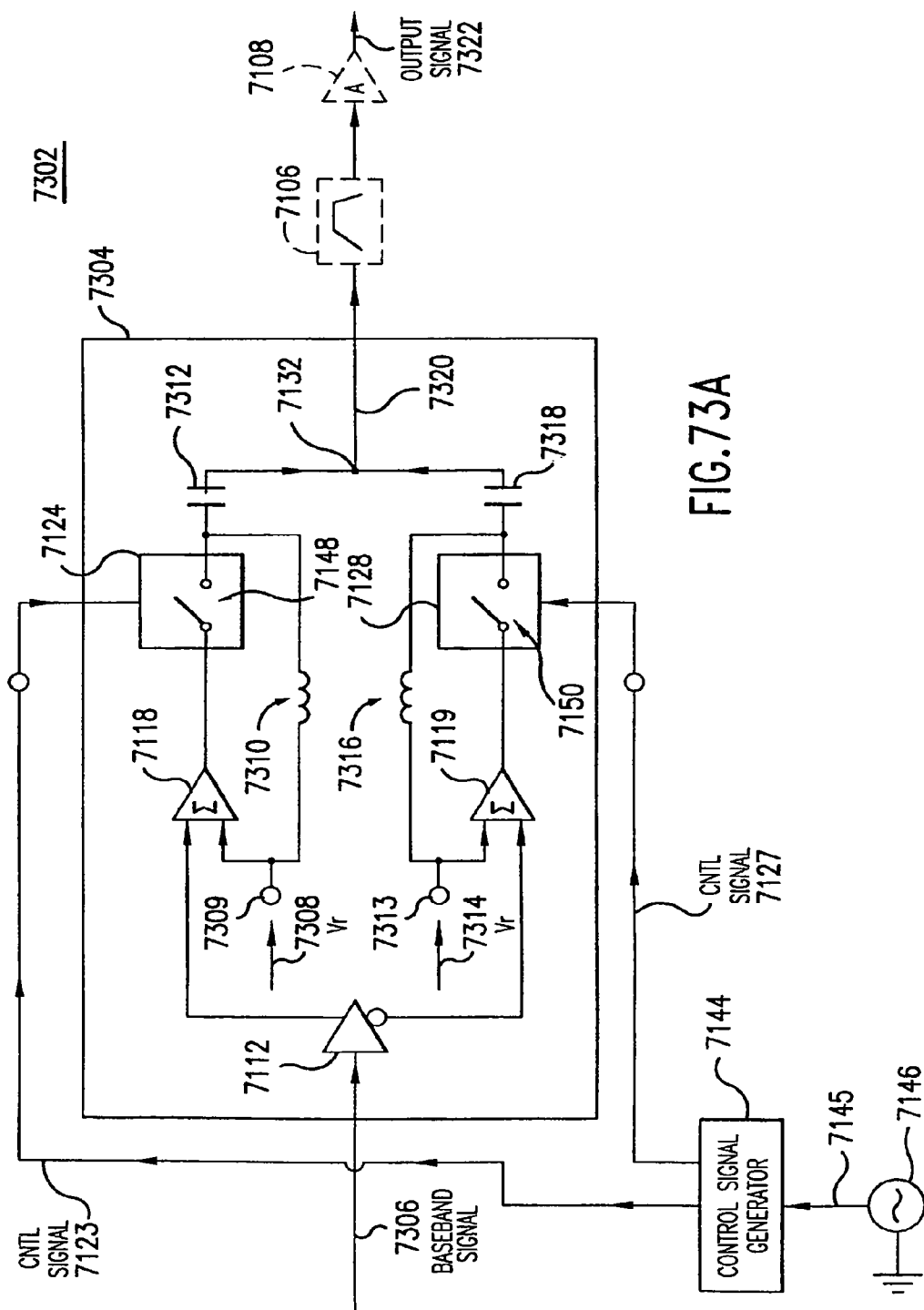


FIG. 73A

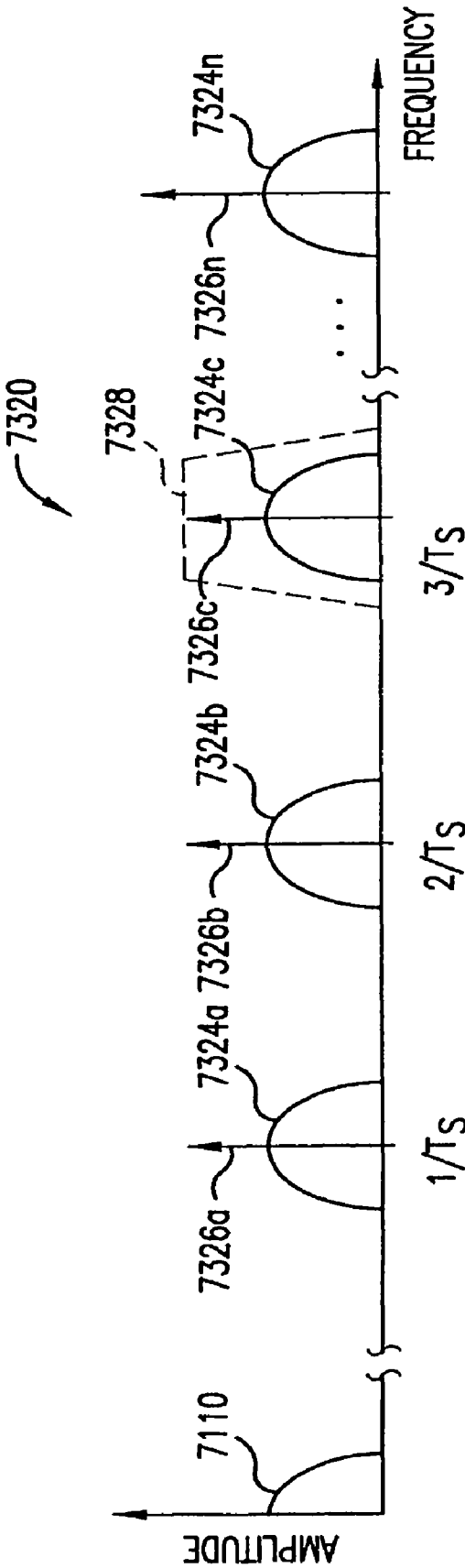


FIG. 73B

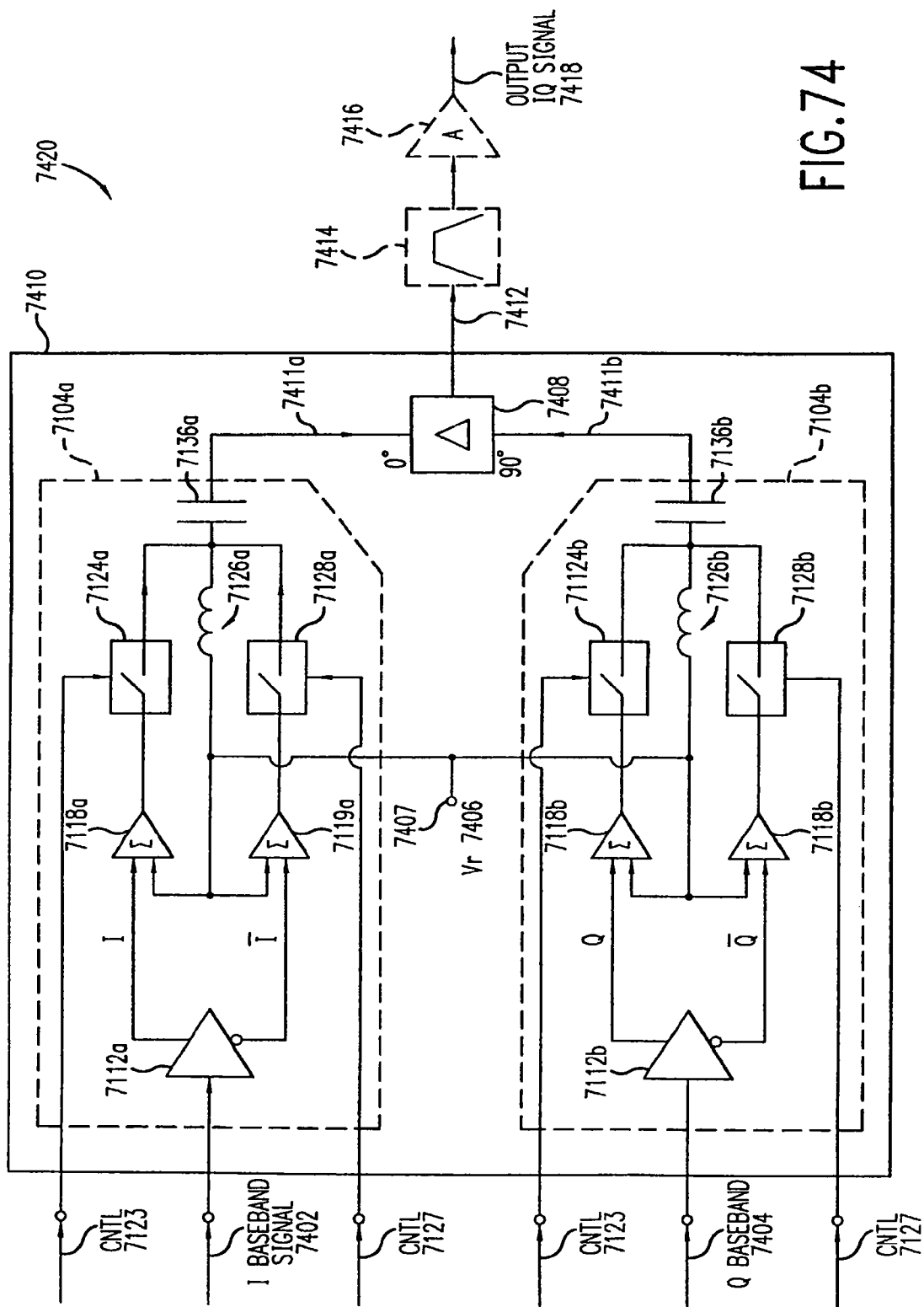
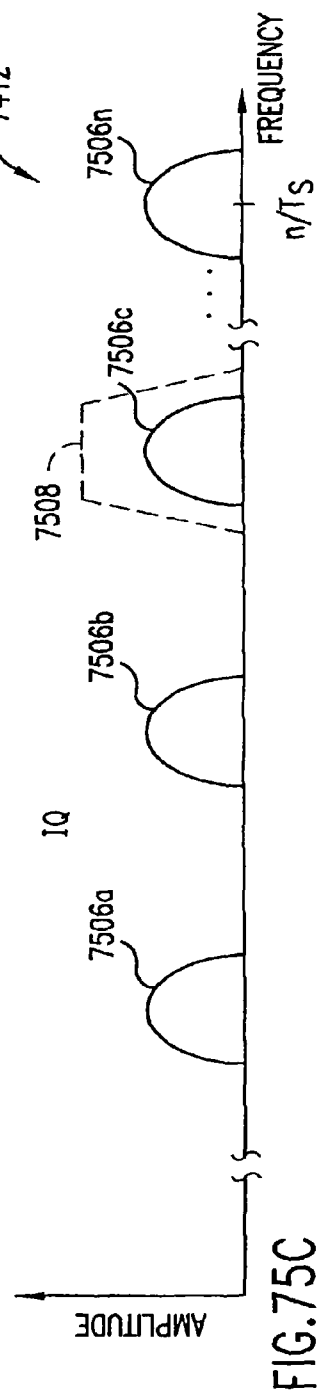
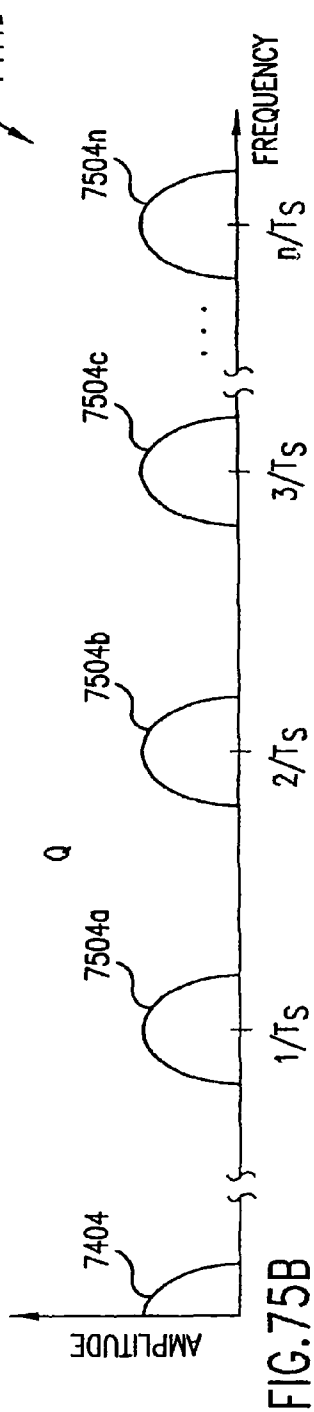
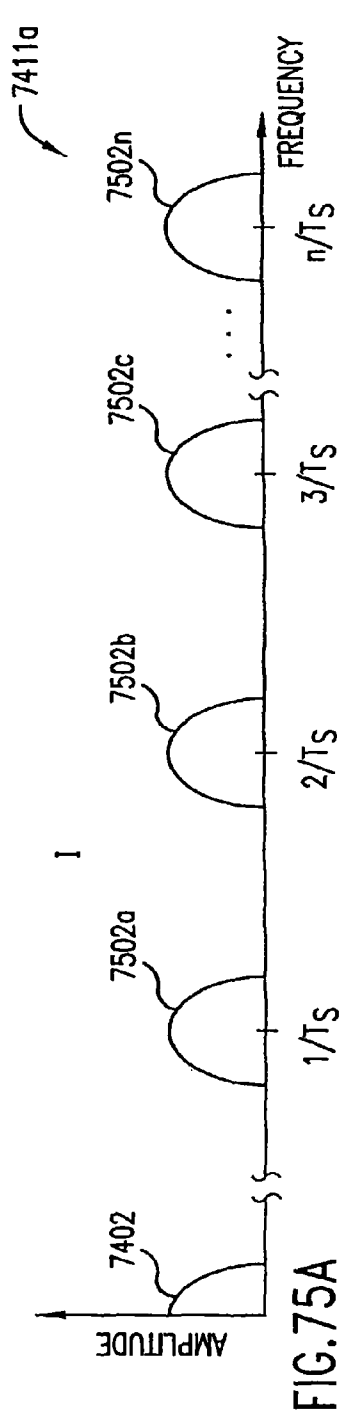


FIG. 74



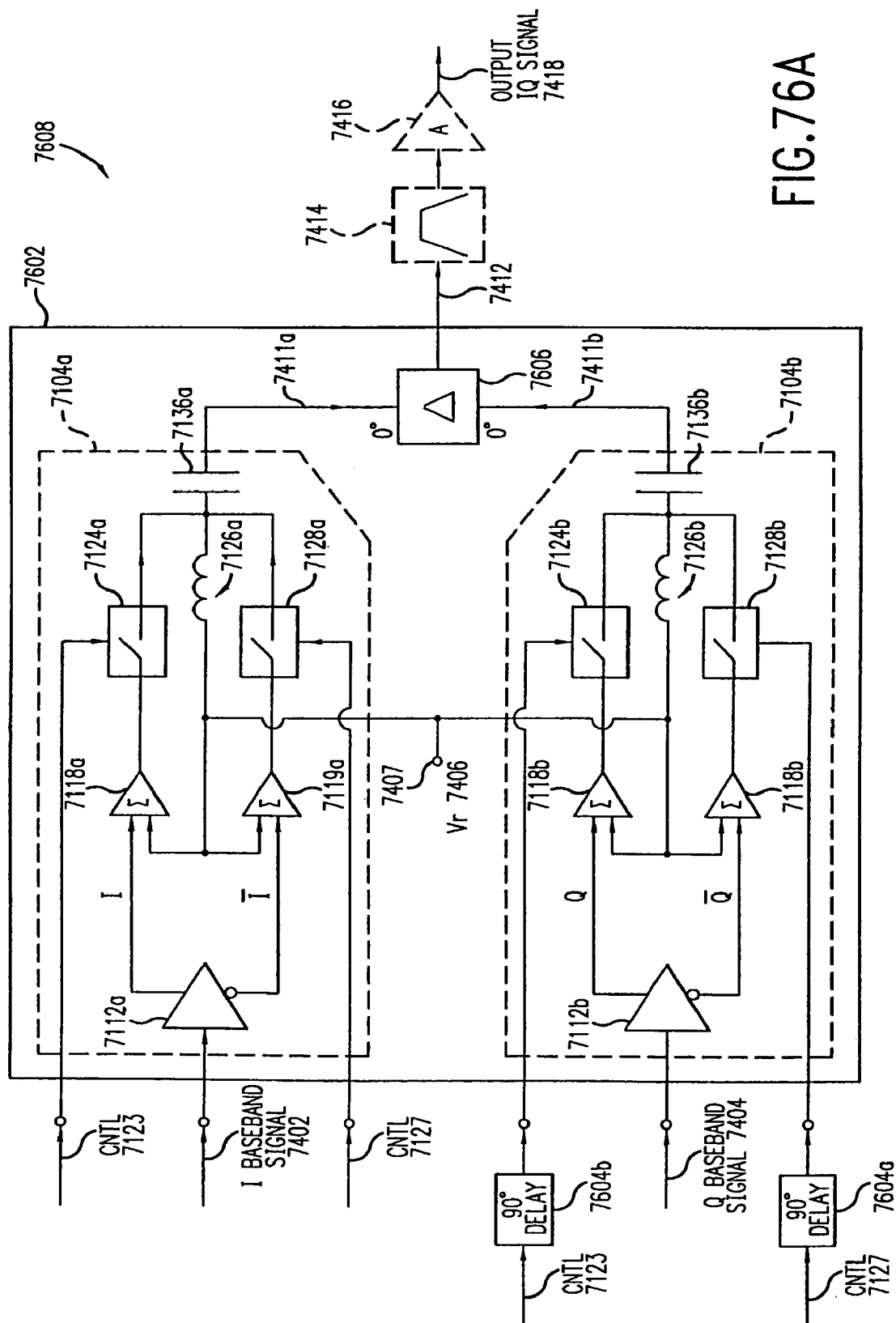


FIG. 76A

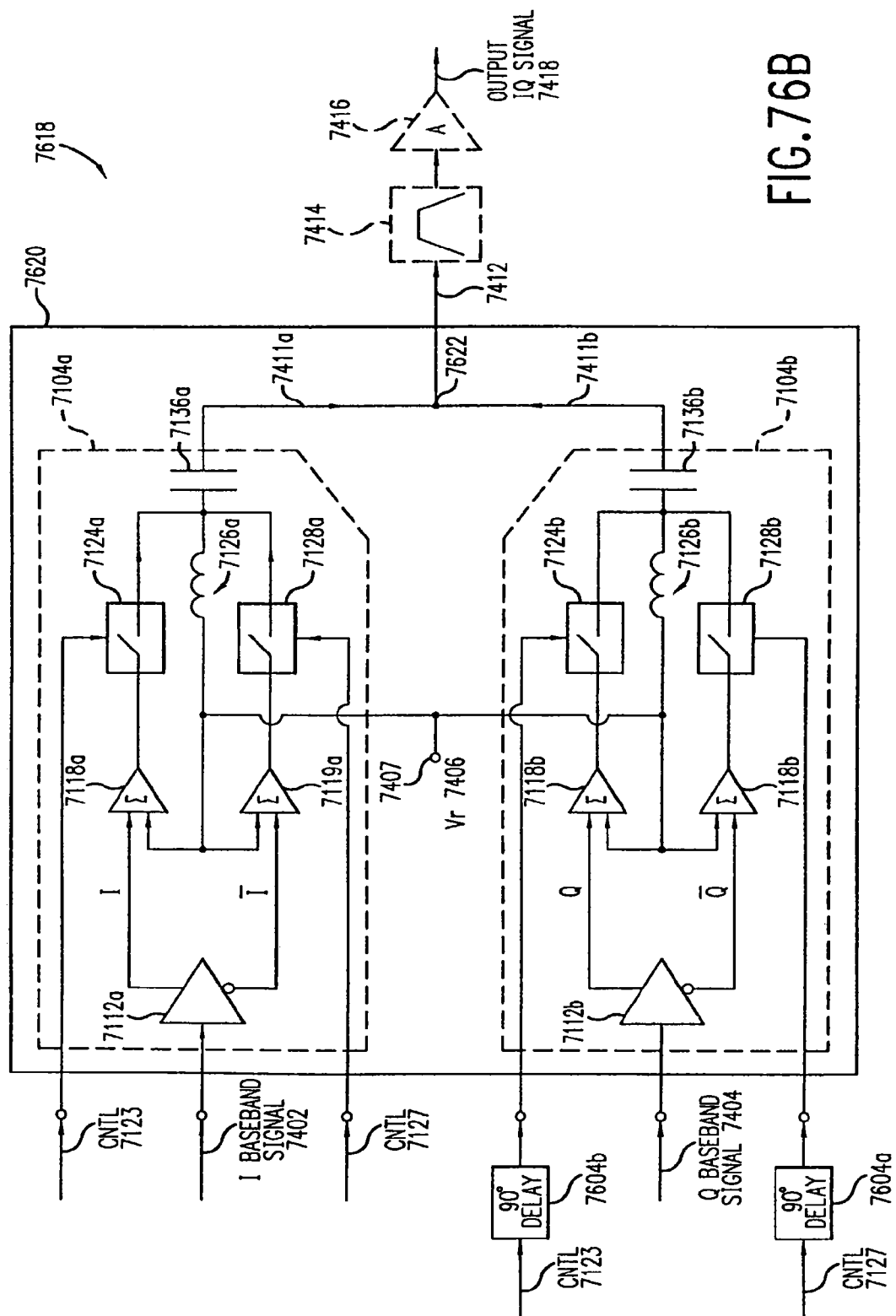
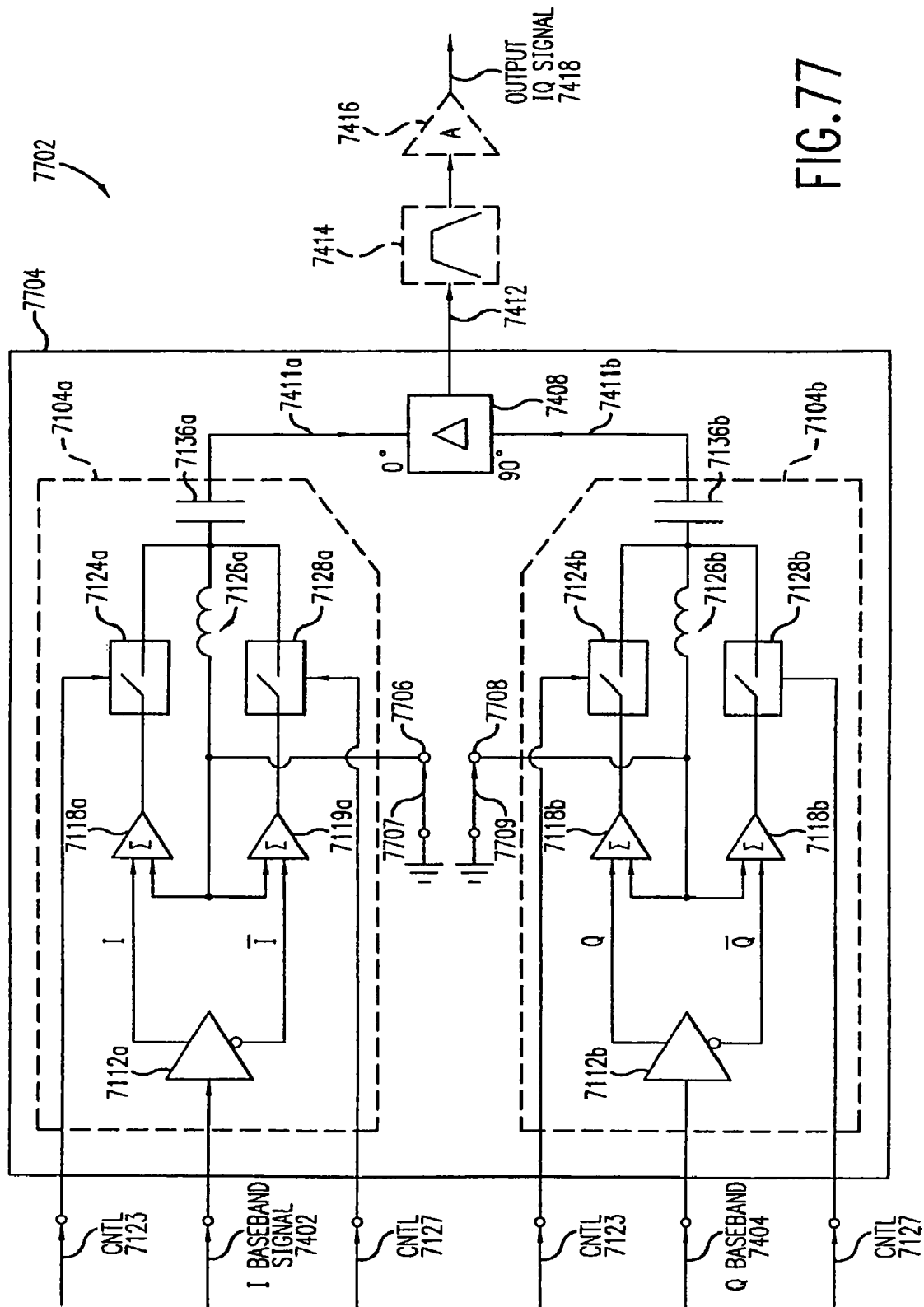


FIG. 76B



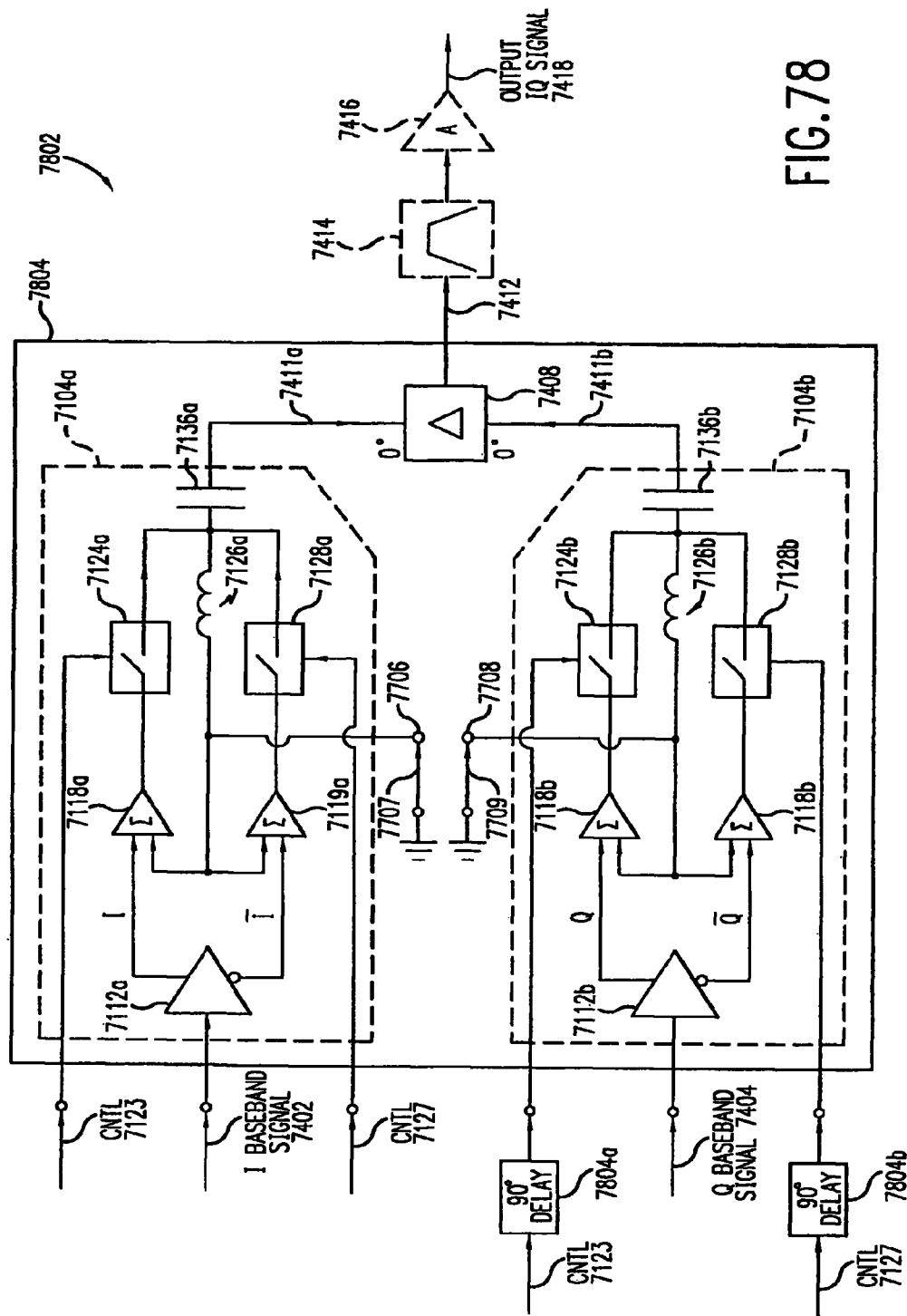
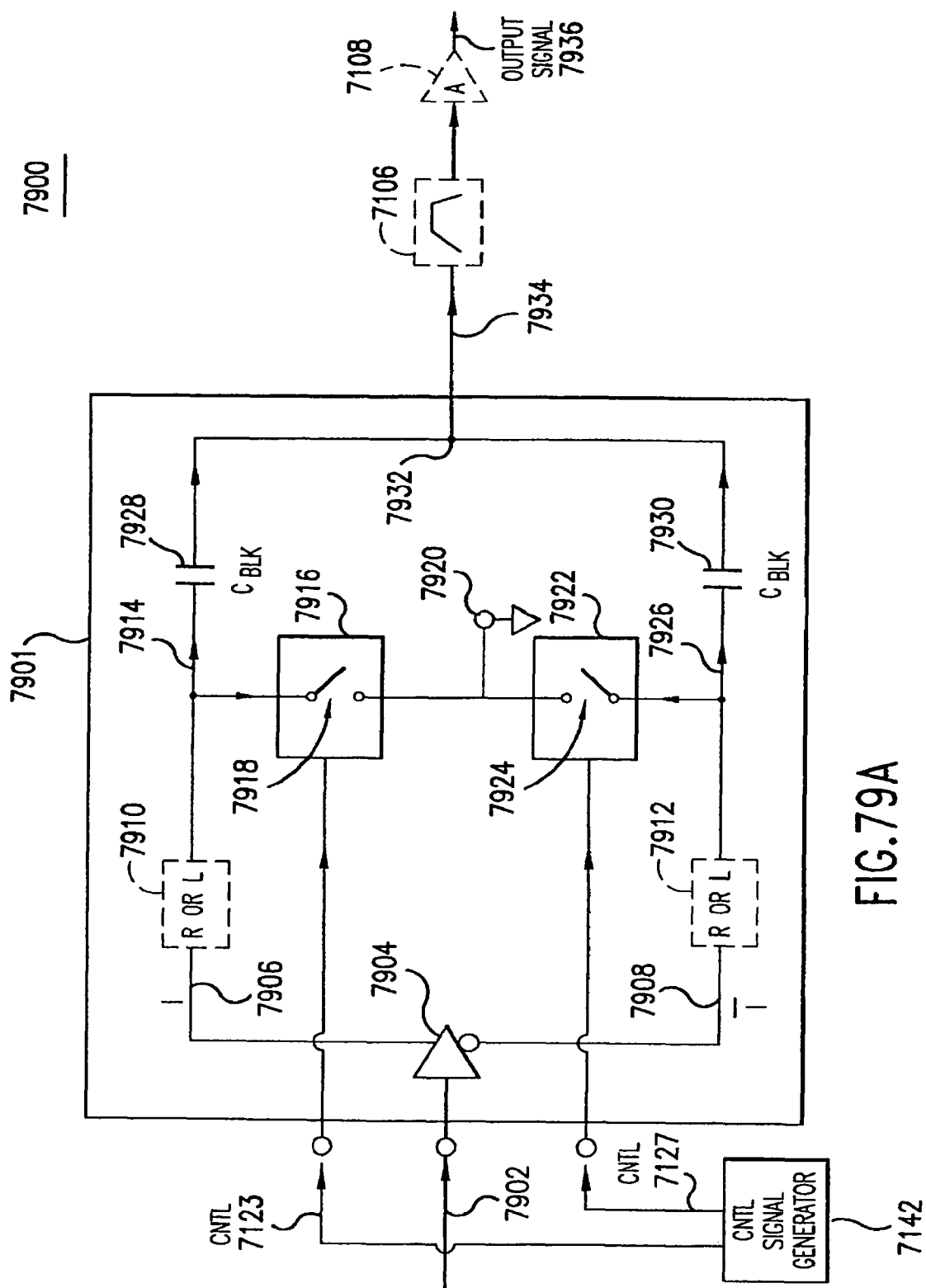


FIG. 78





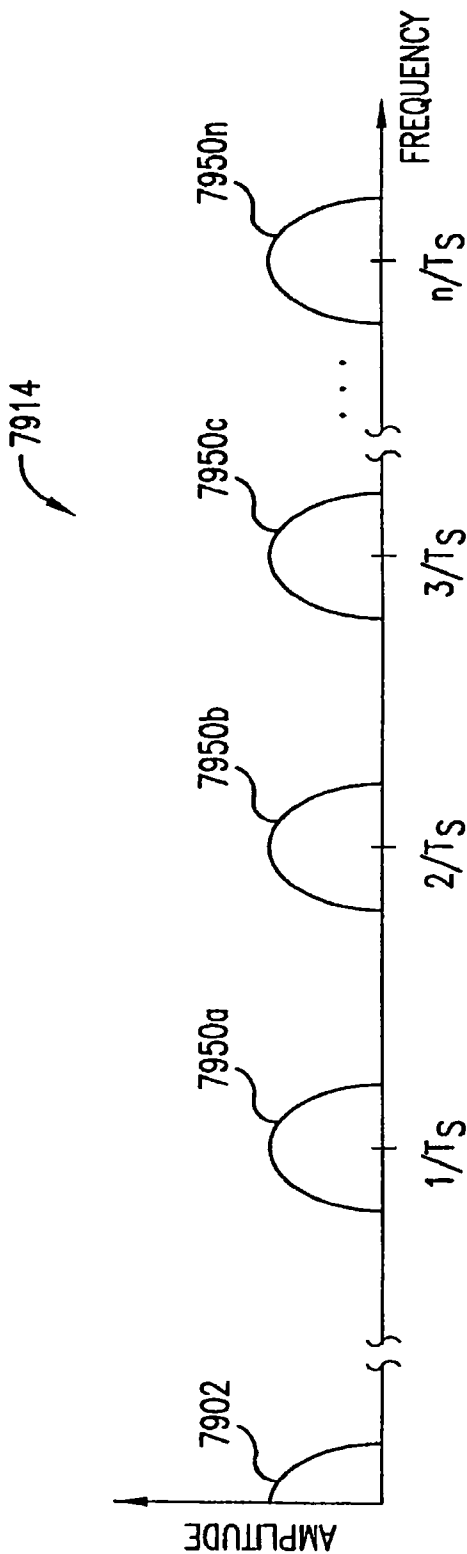


FIG. 7914

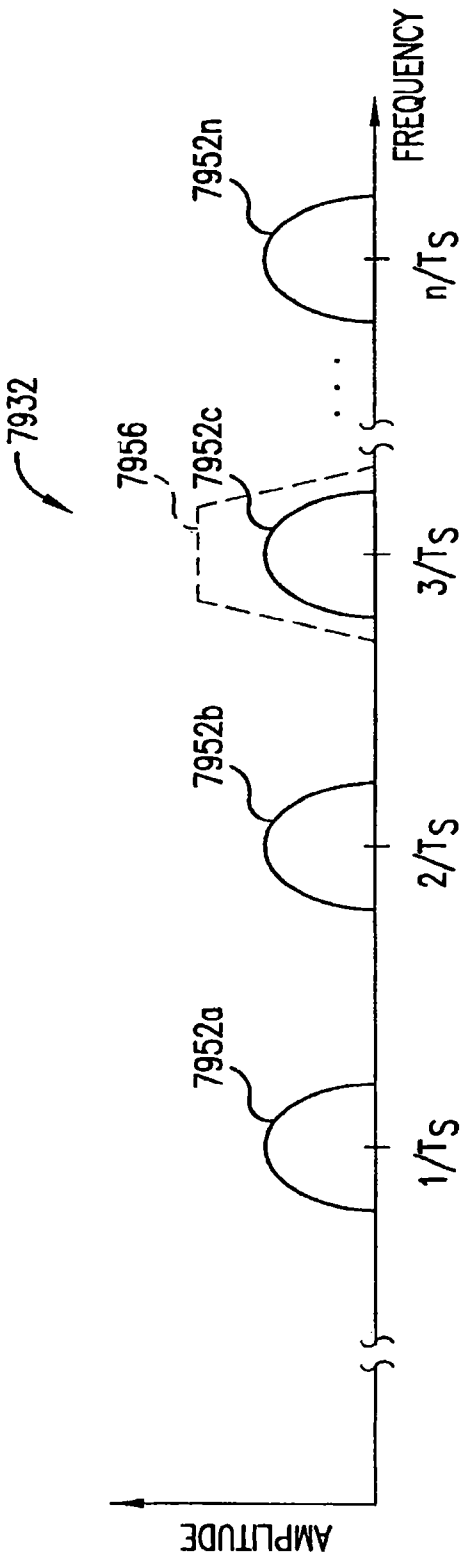
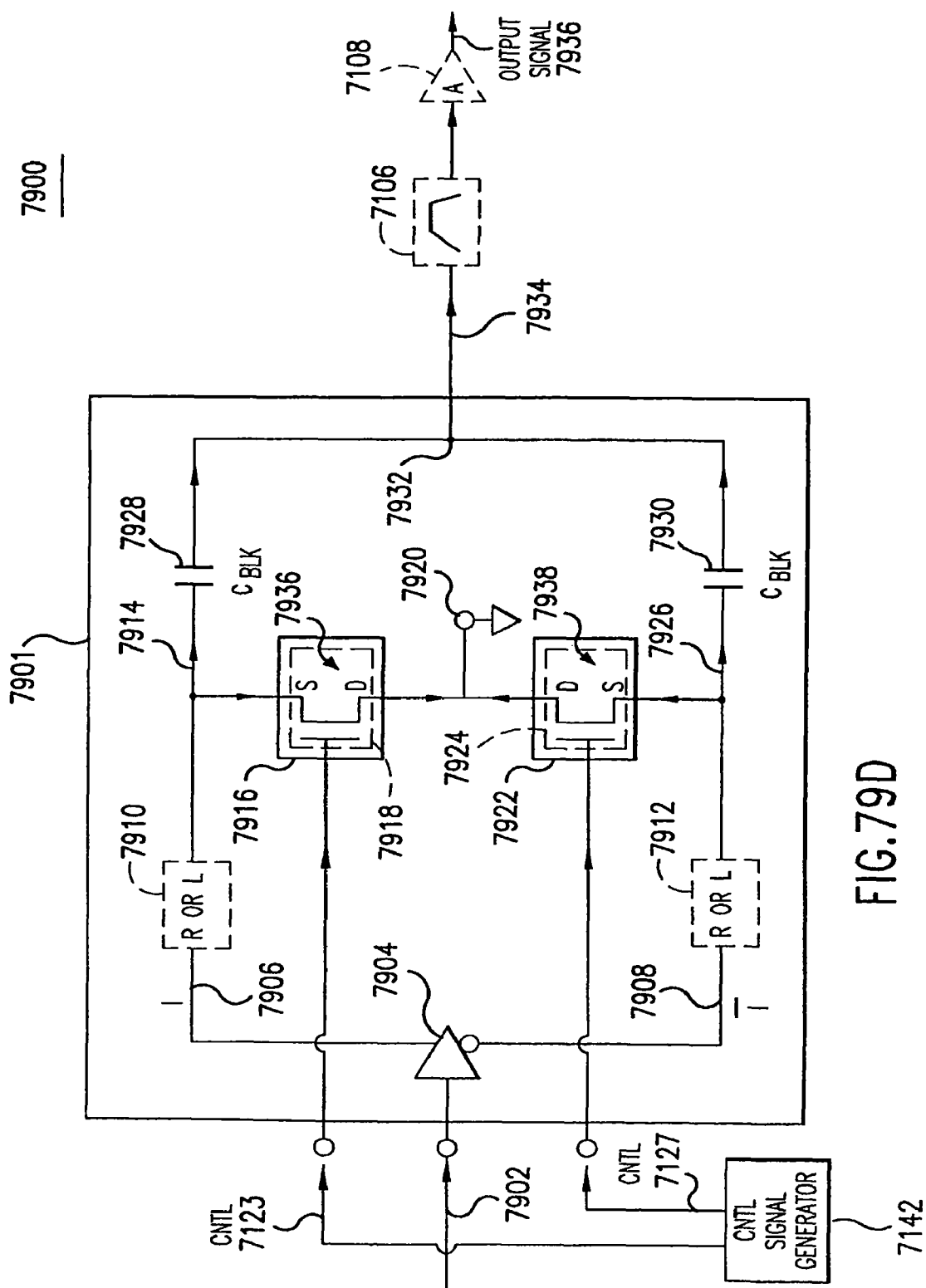
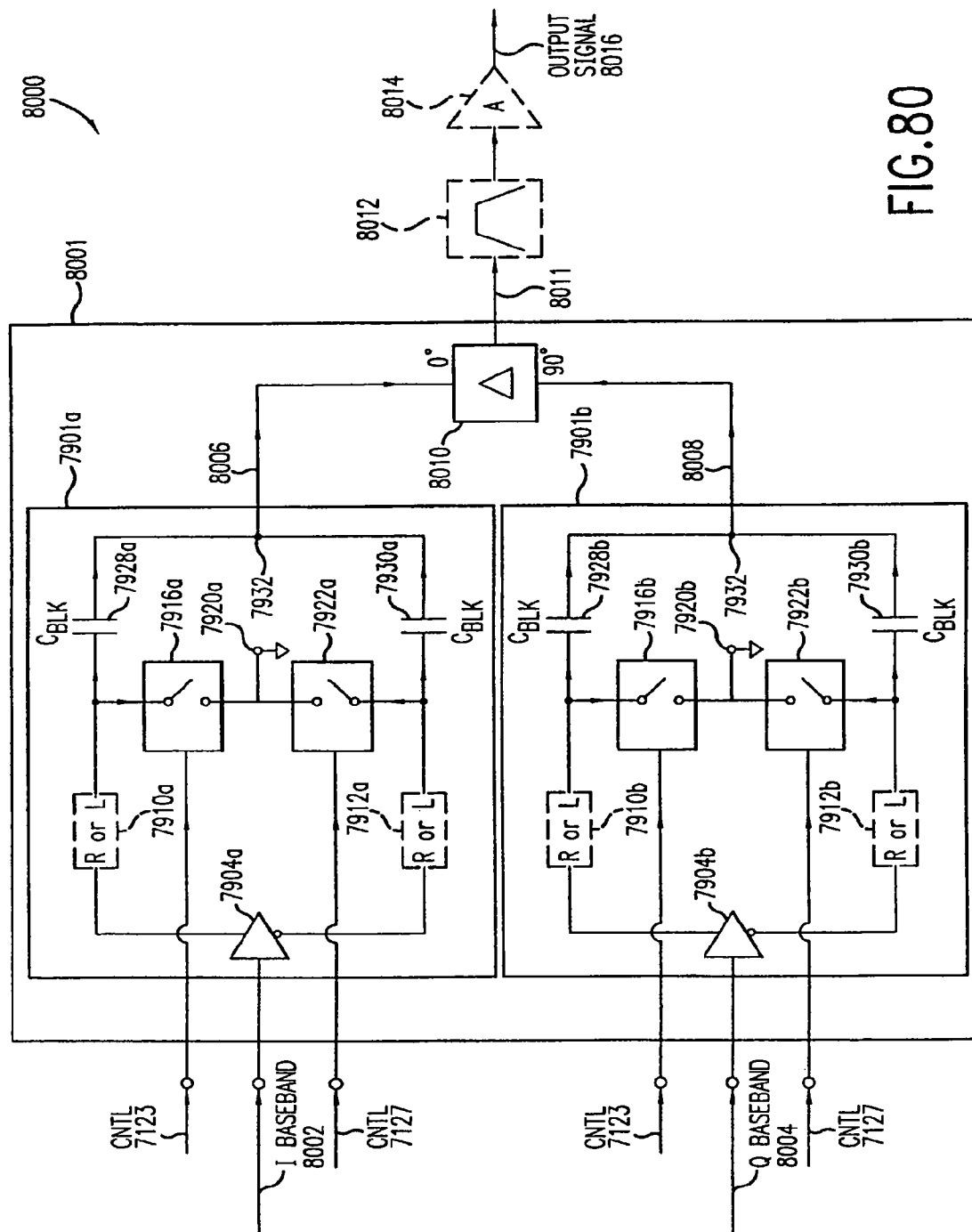
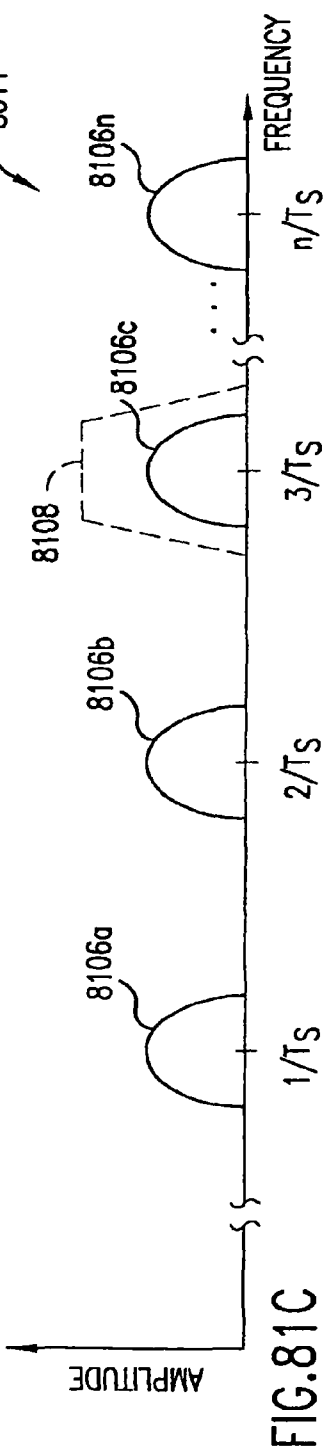
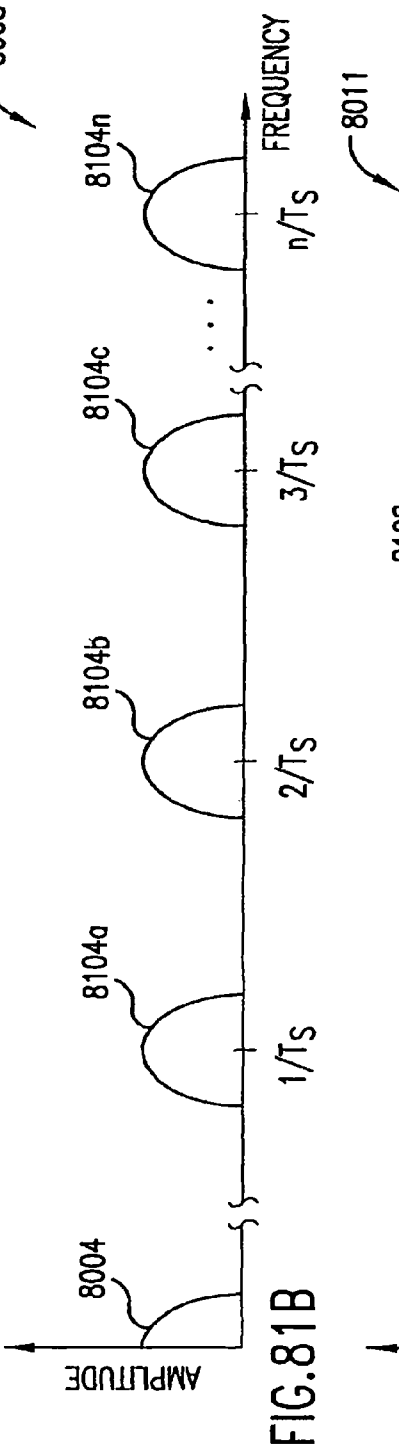
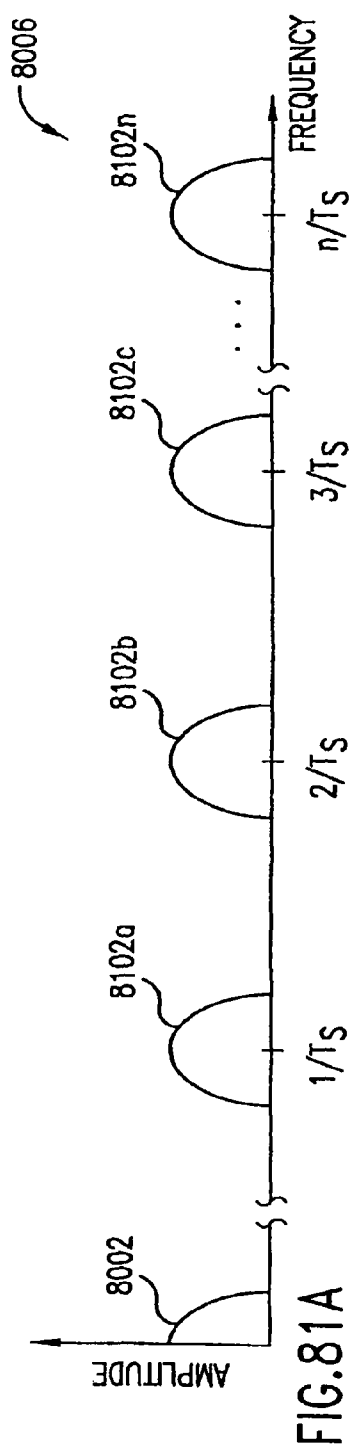


FIG. 7932







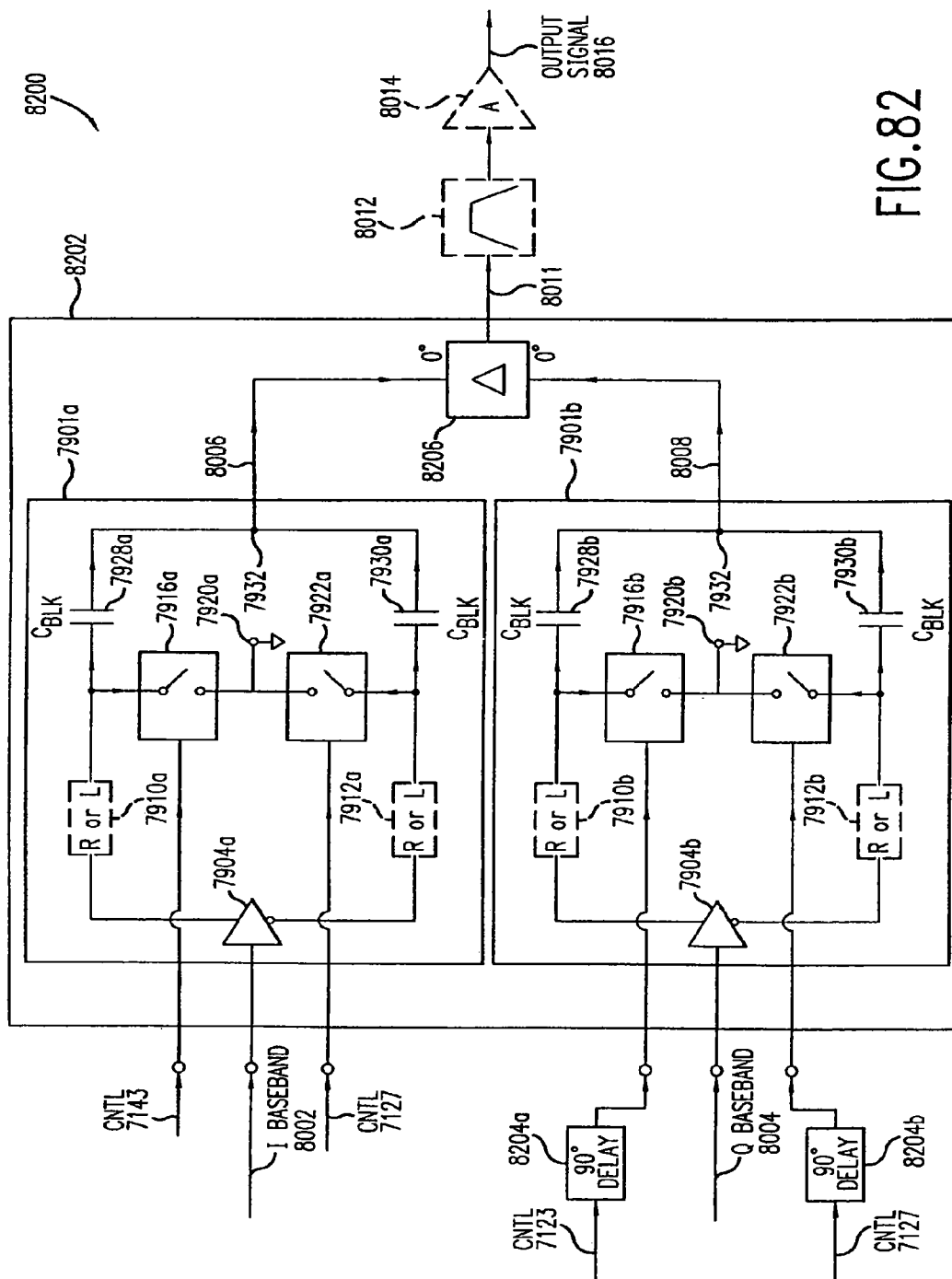


FIG. 82

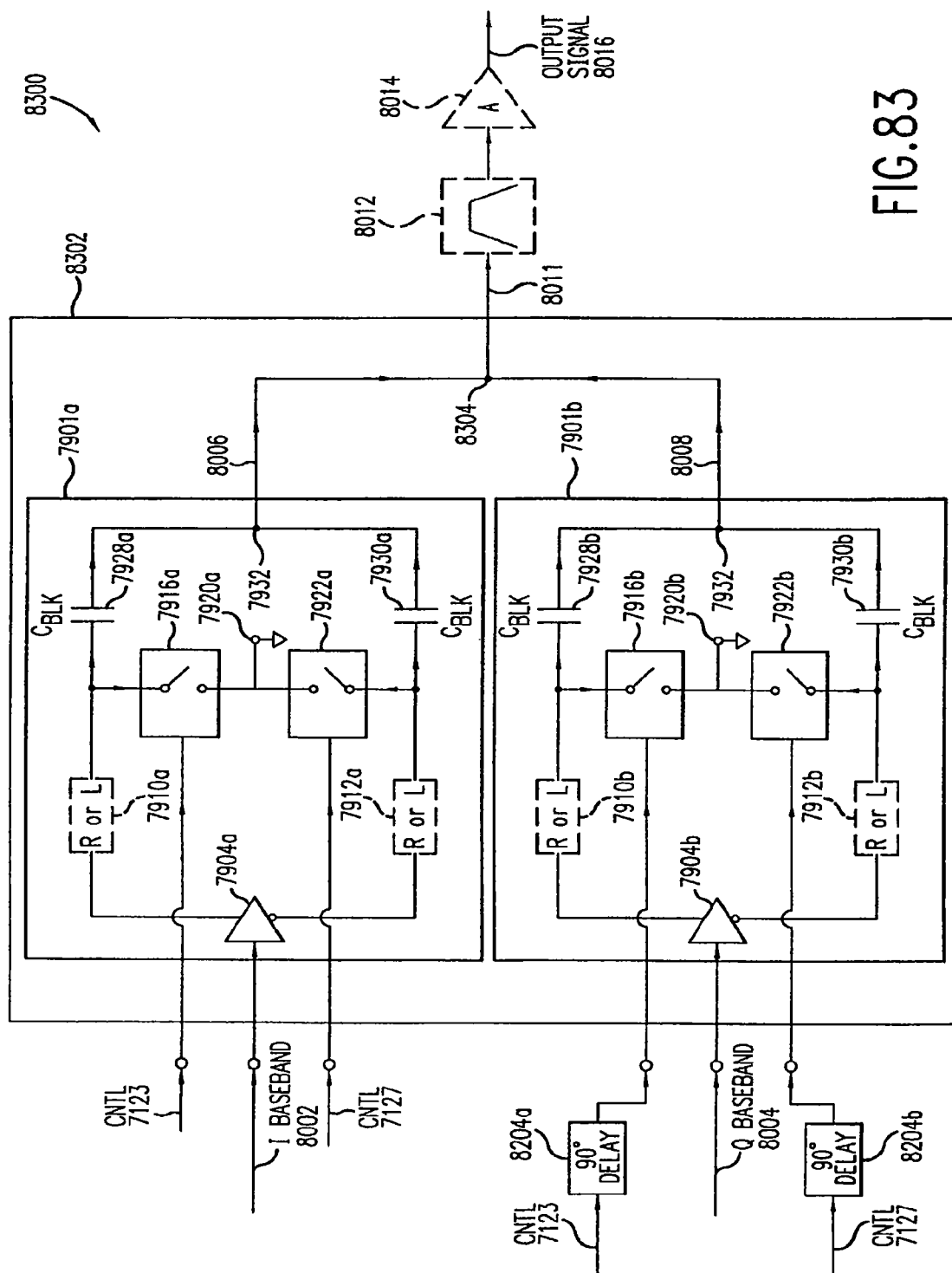


FIG.83

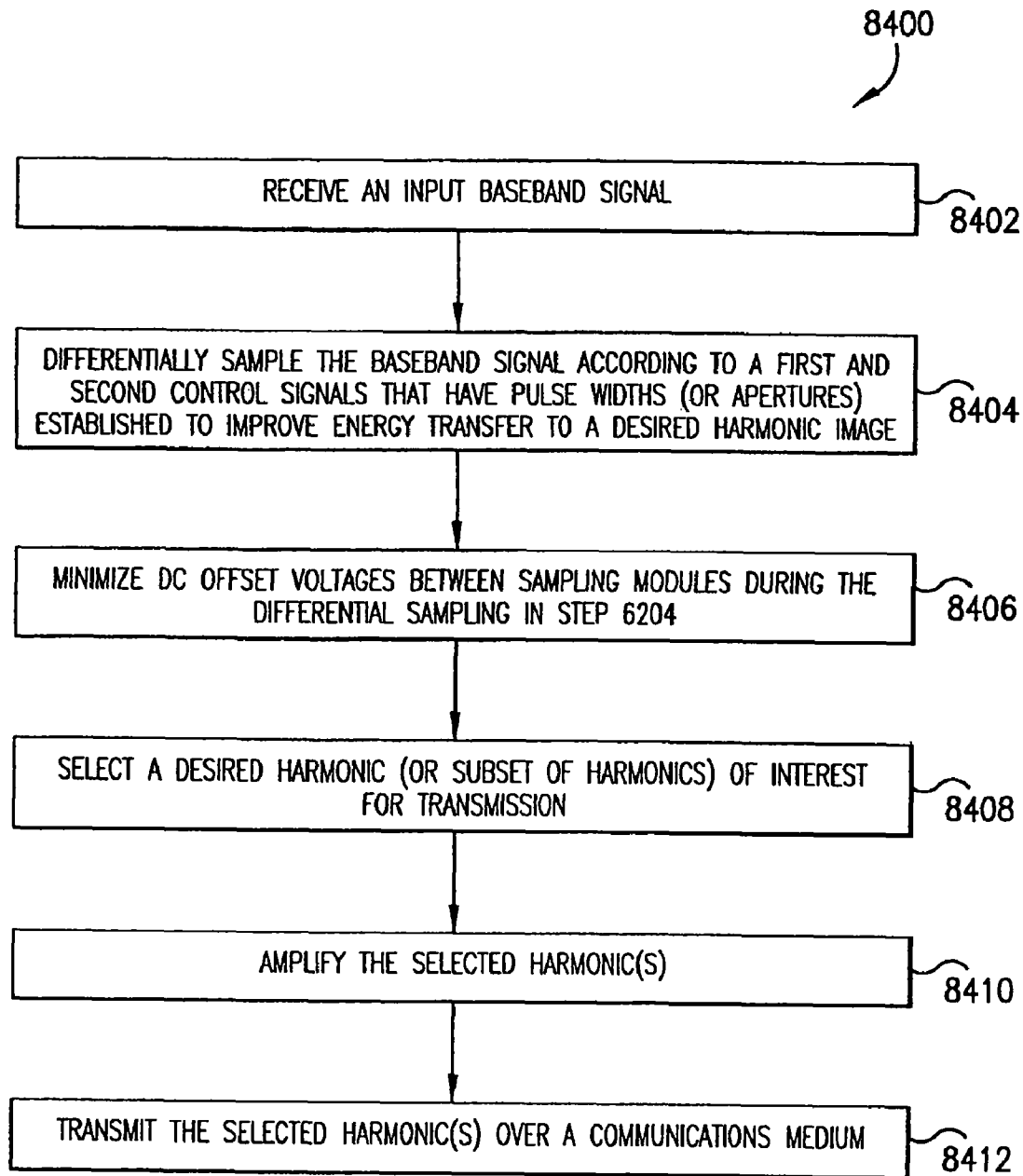


FIG.84



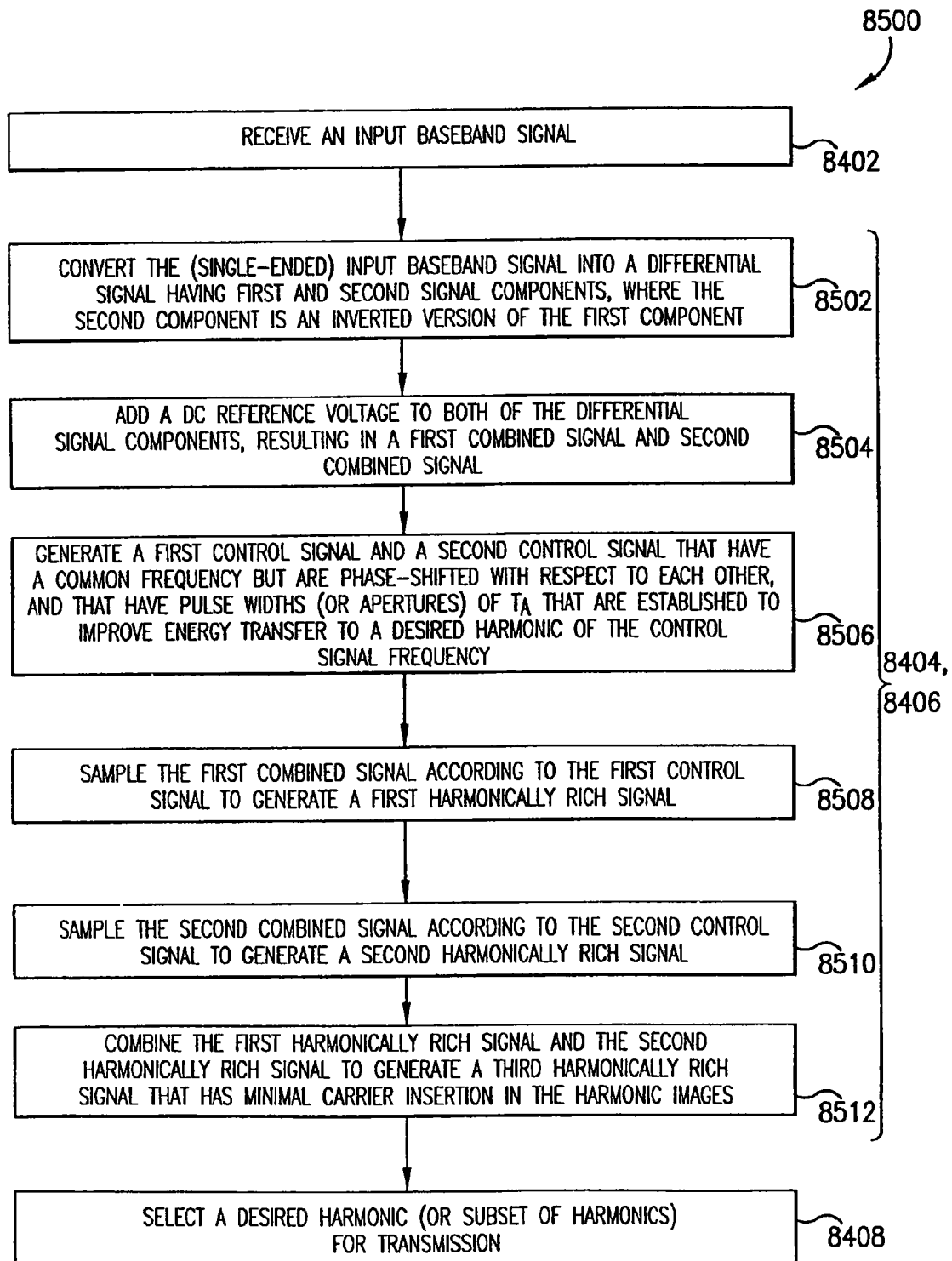


FIG.85

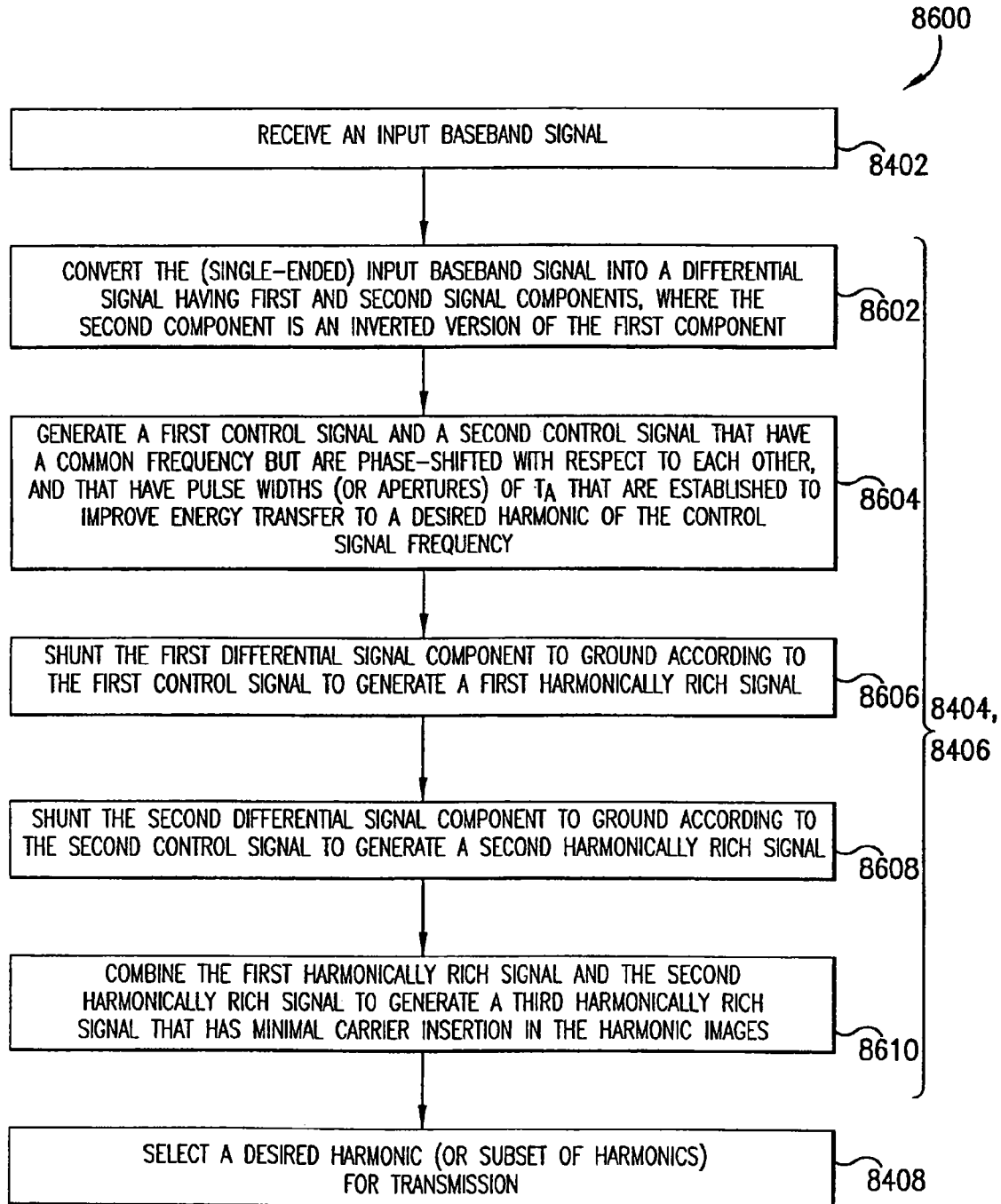


FIG.86

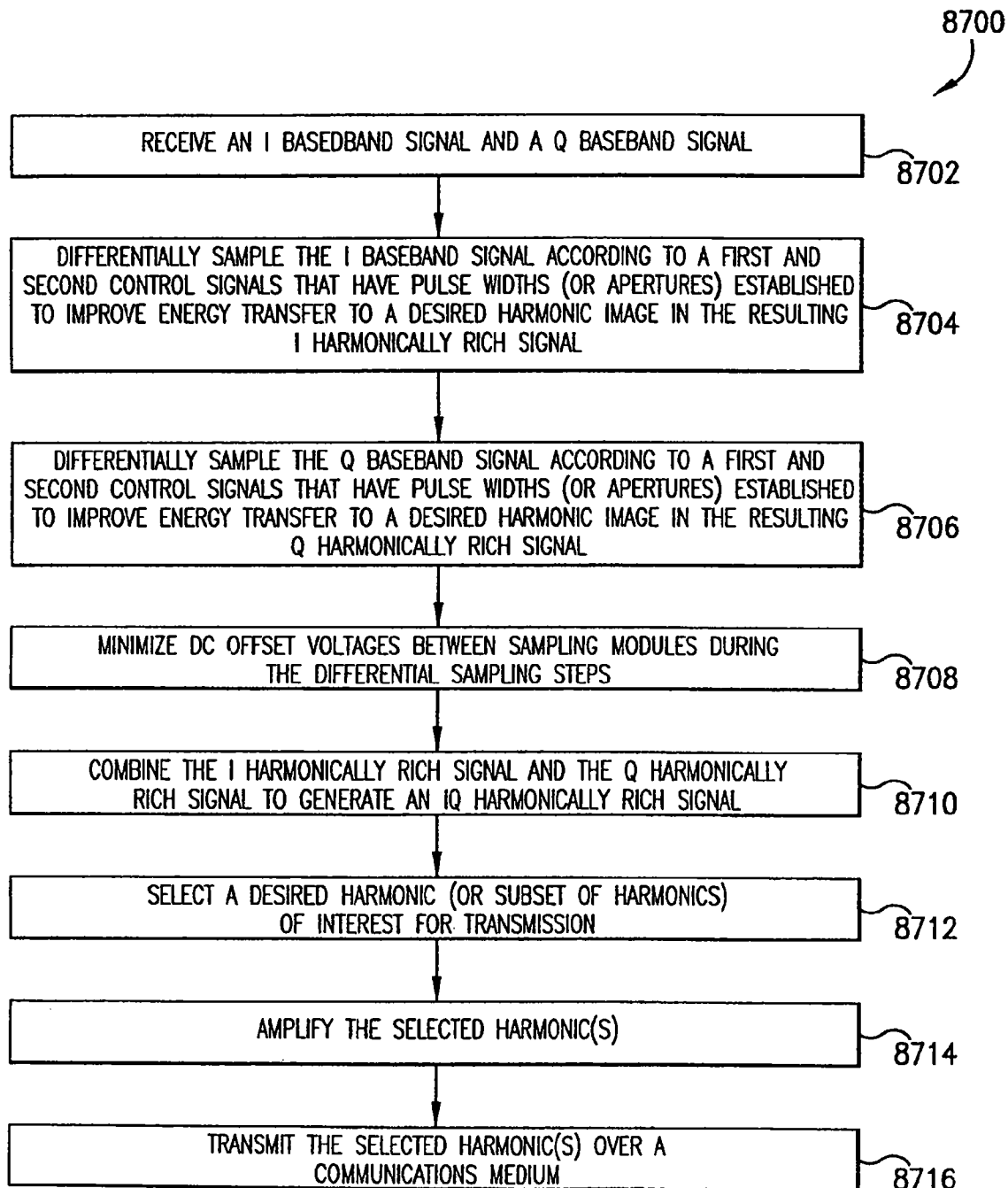


FIG.87

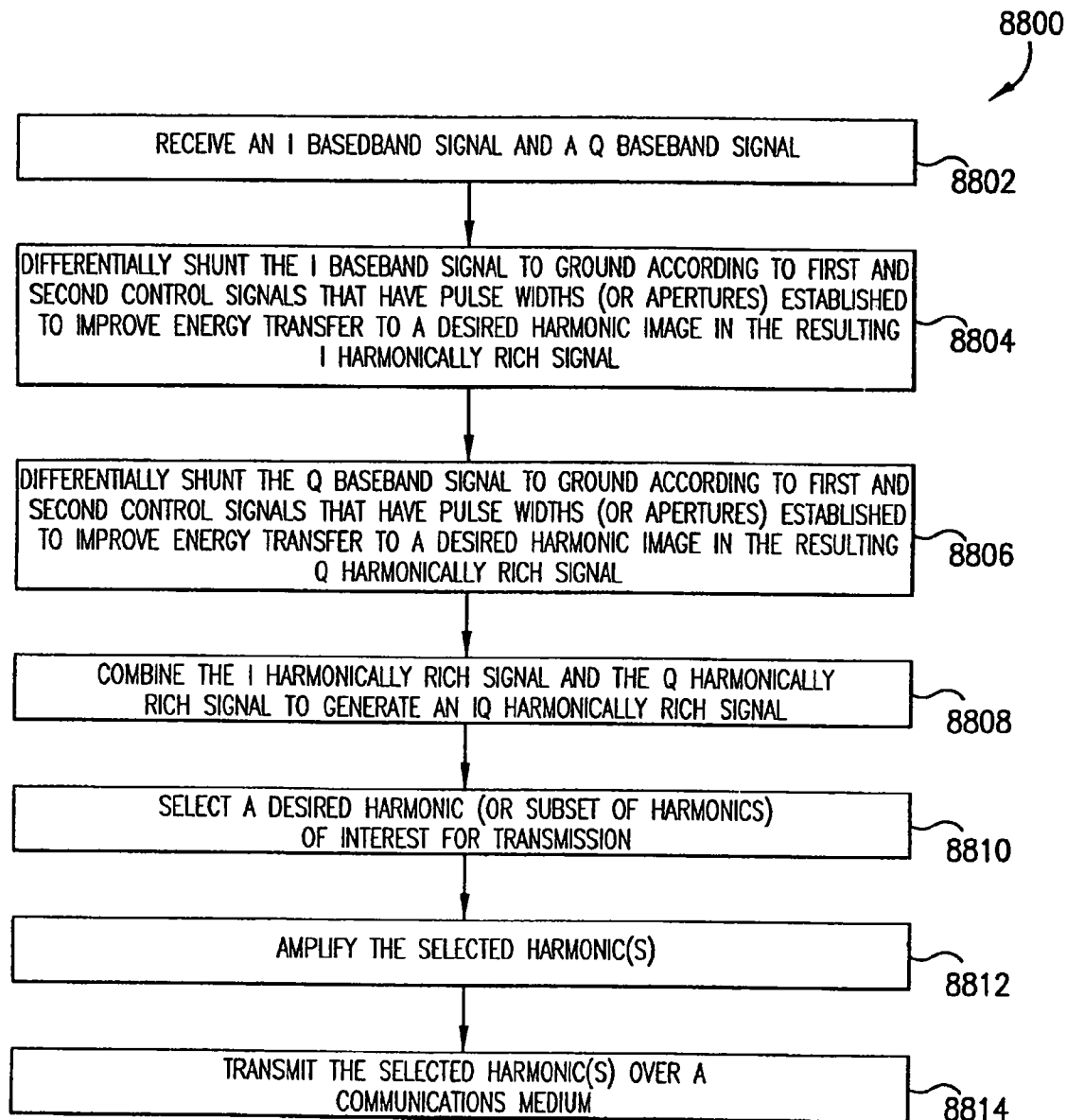


FIG.88

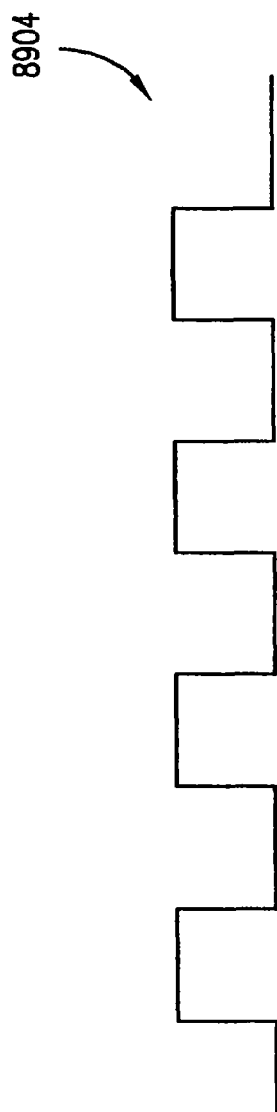
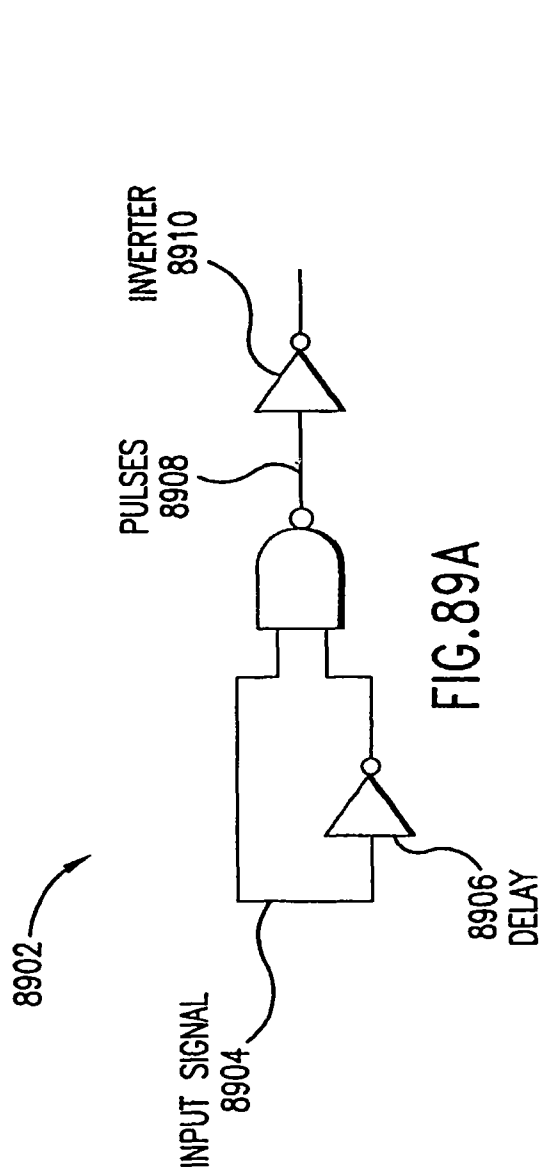


FIG. 89B

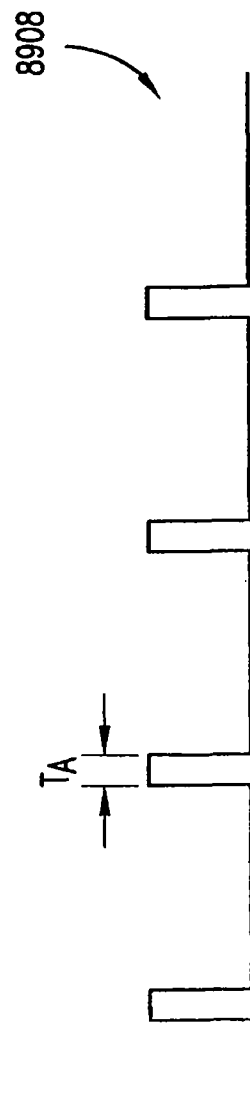


FIG. 89C

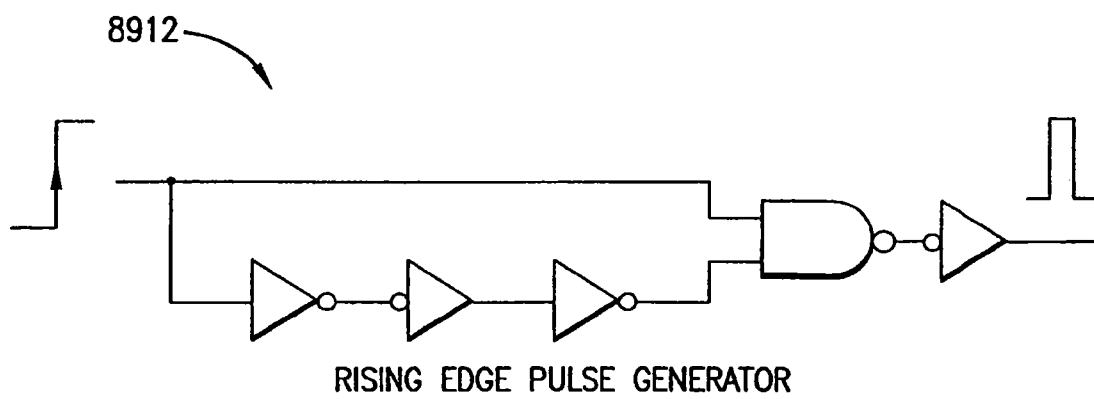


FIG. 89D

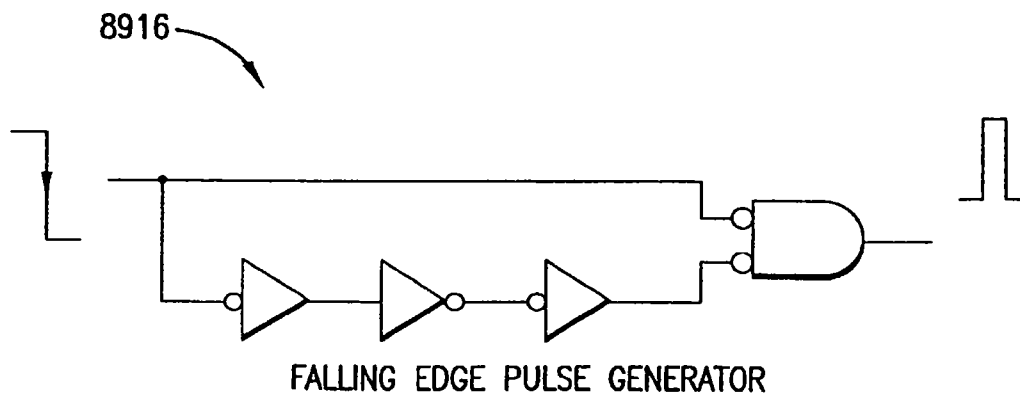
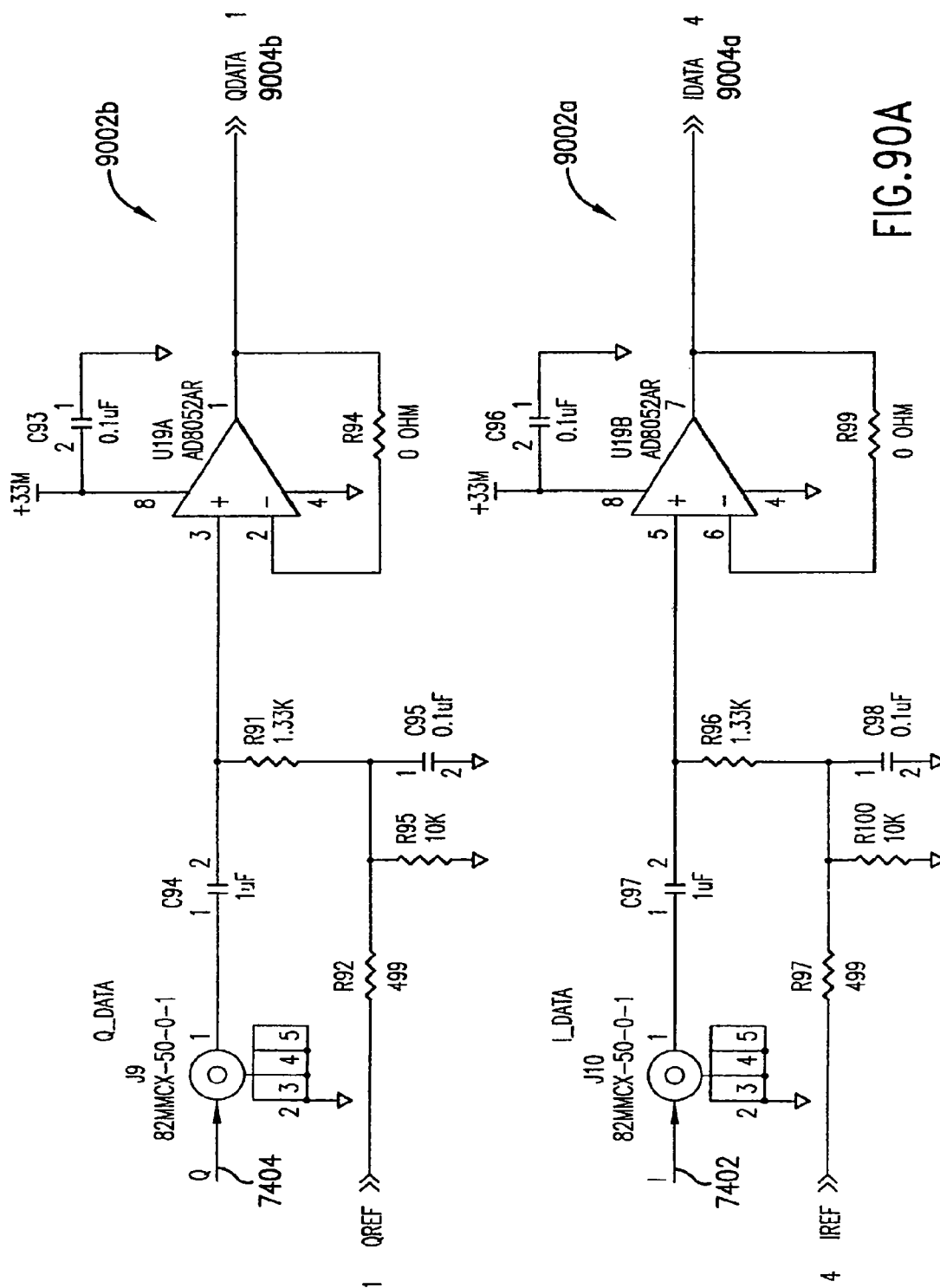


FIG. 89E



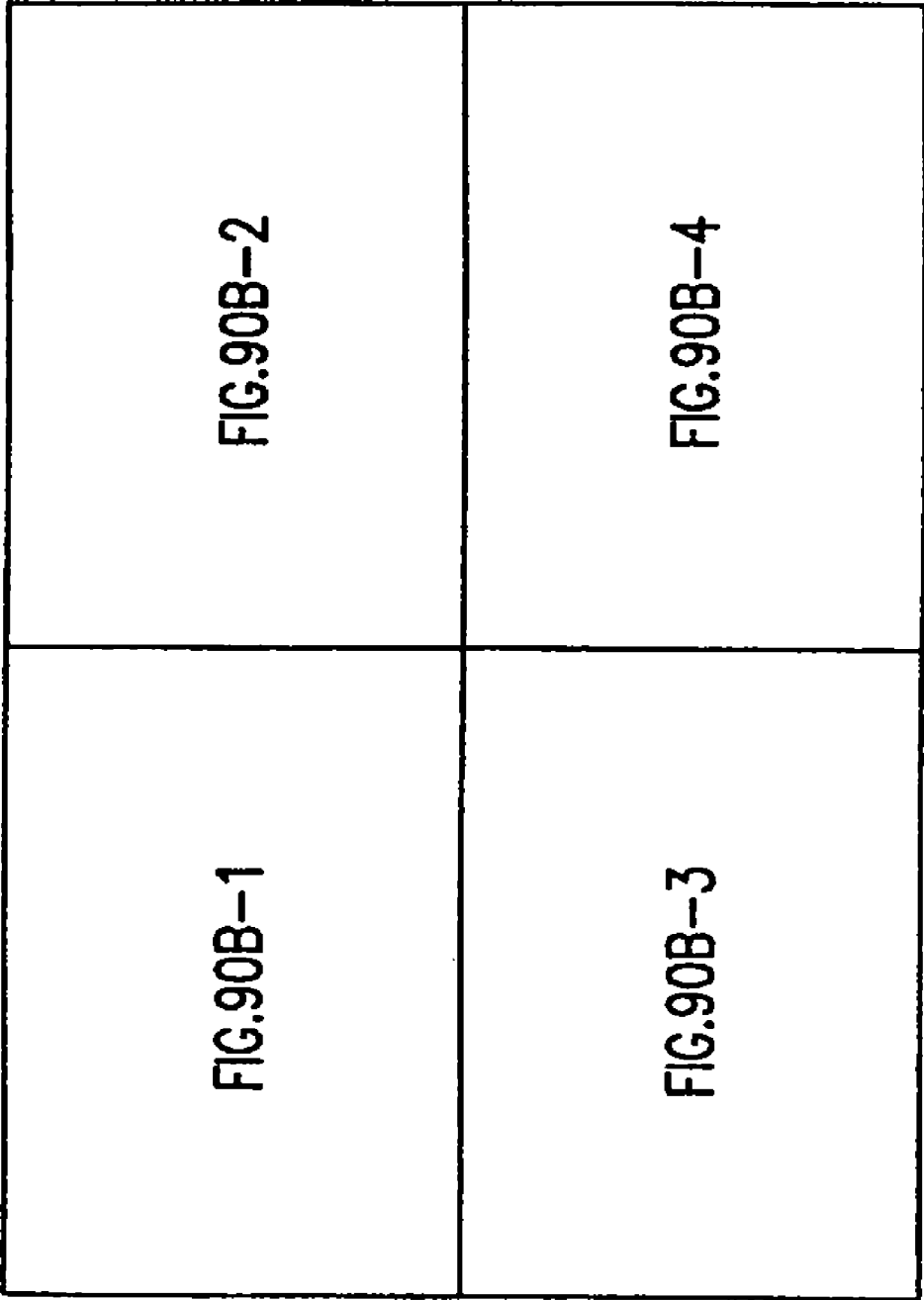


FIG. 90B



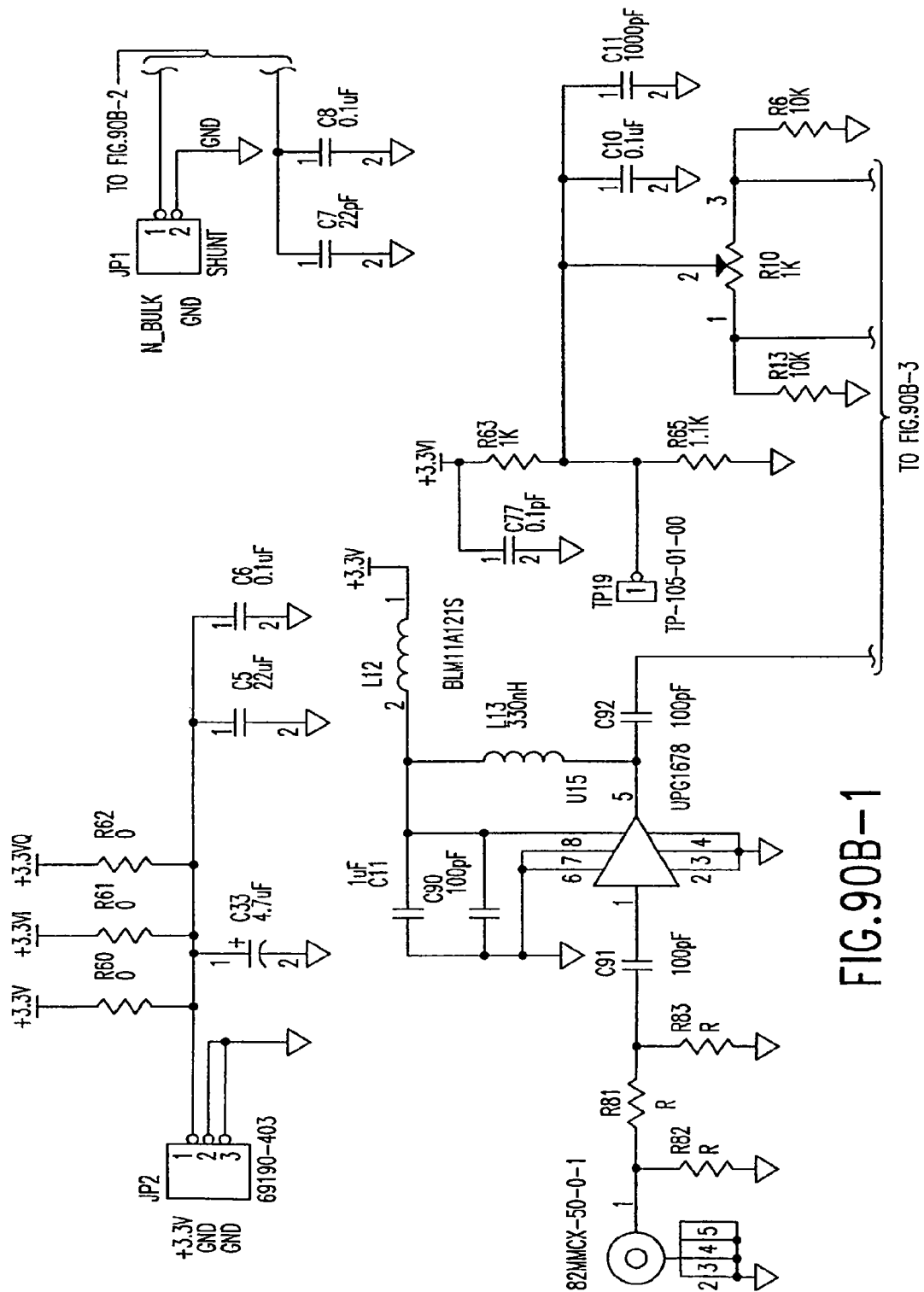
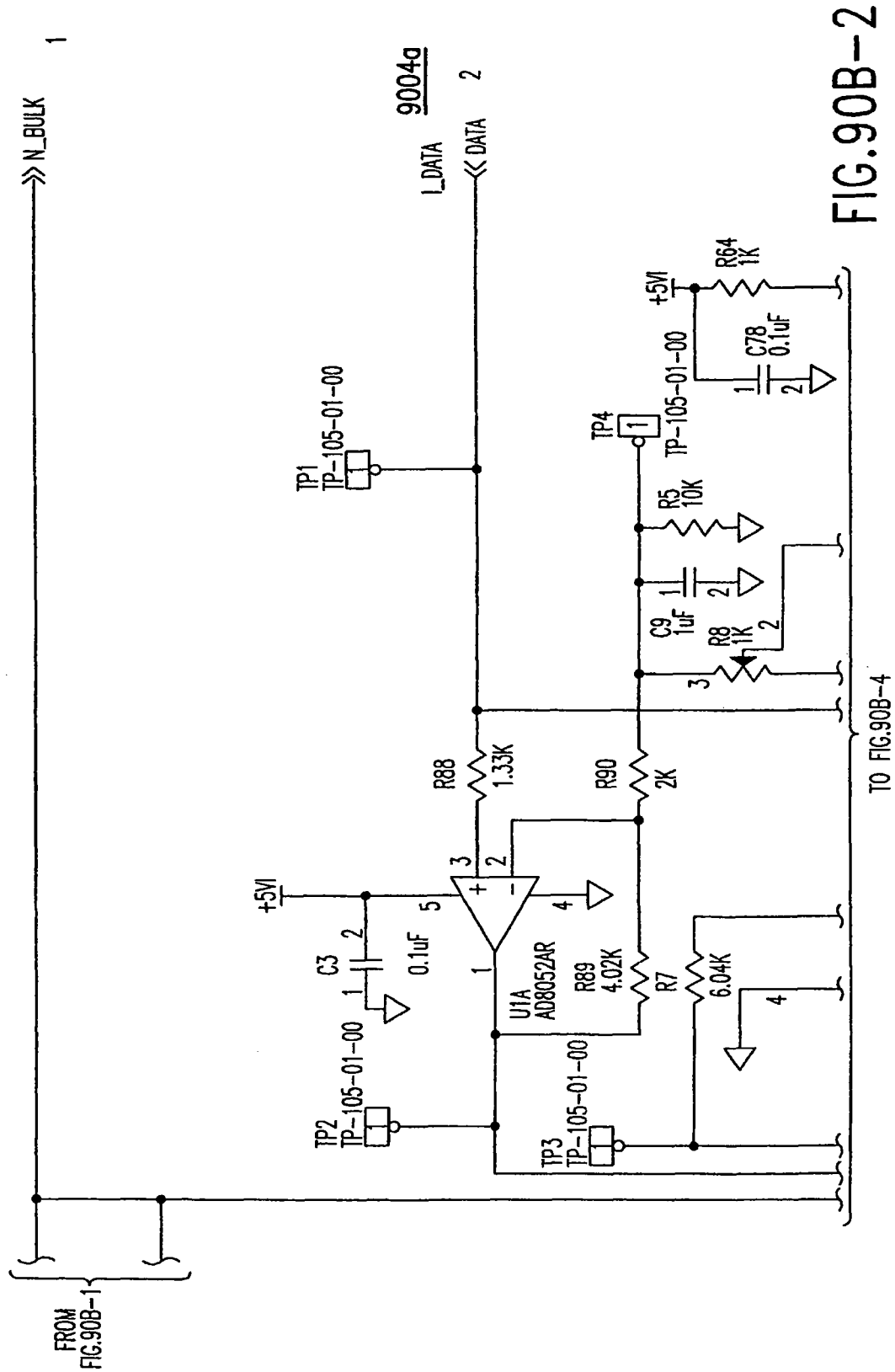


FIG. 90B-1



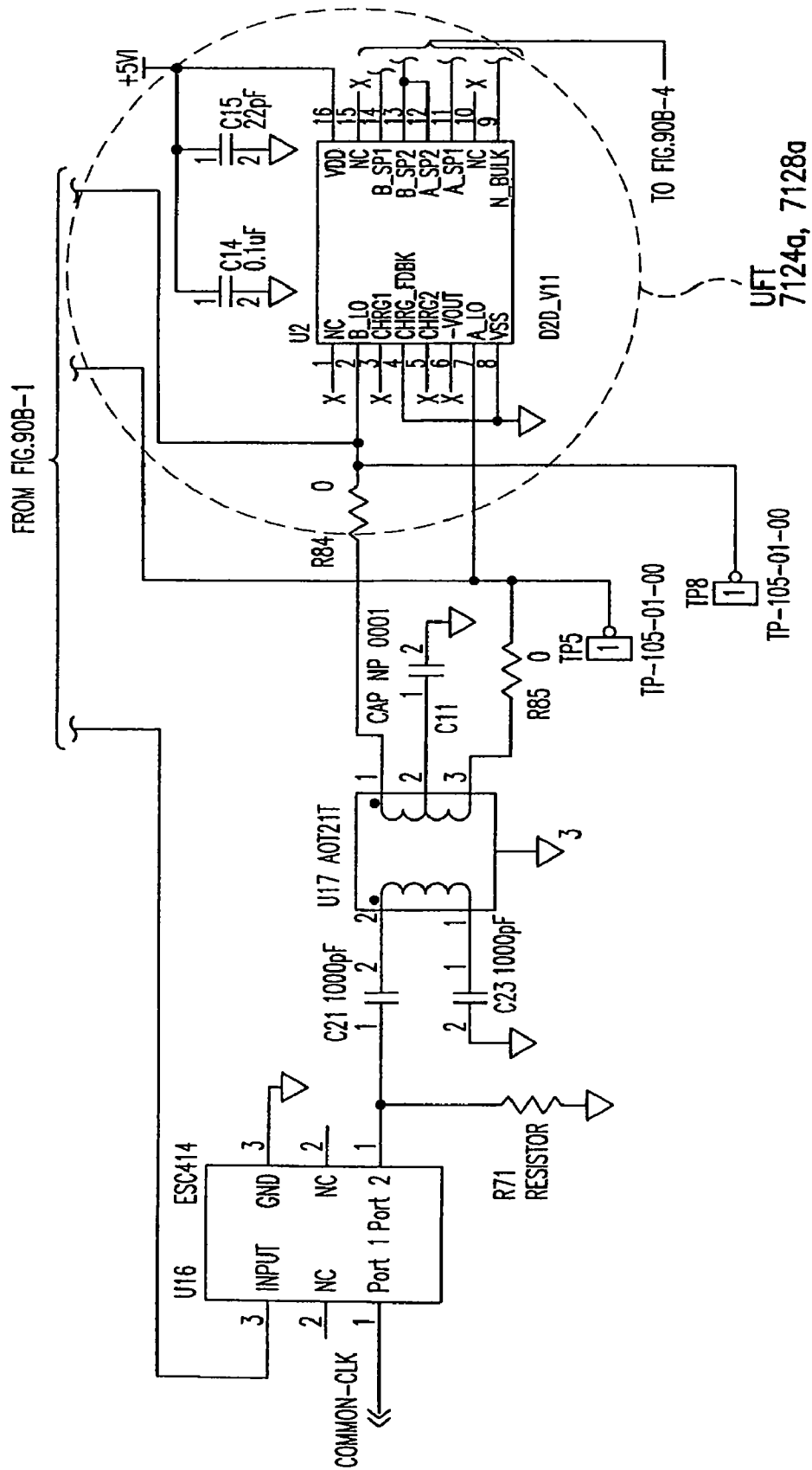
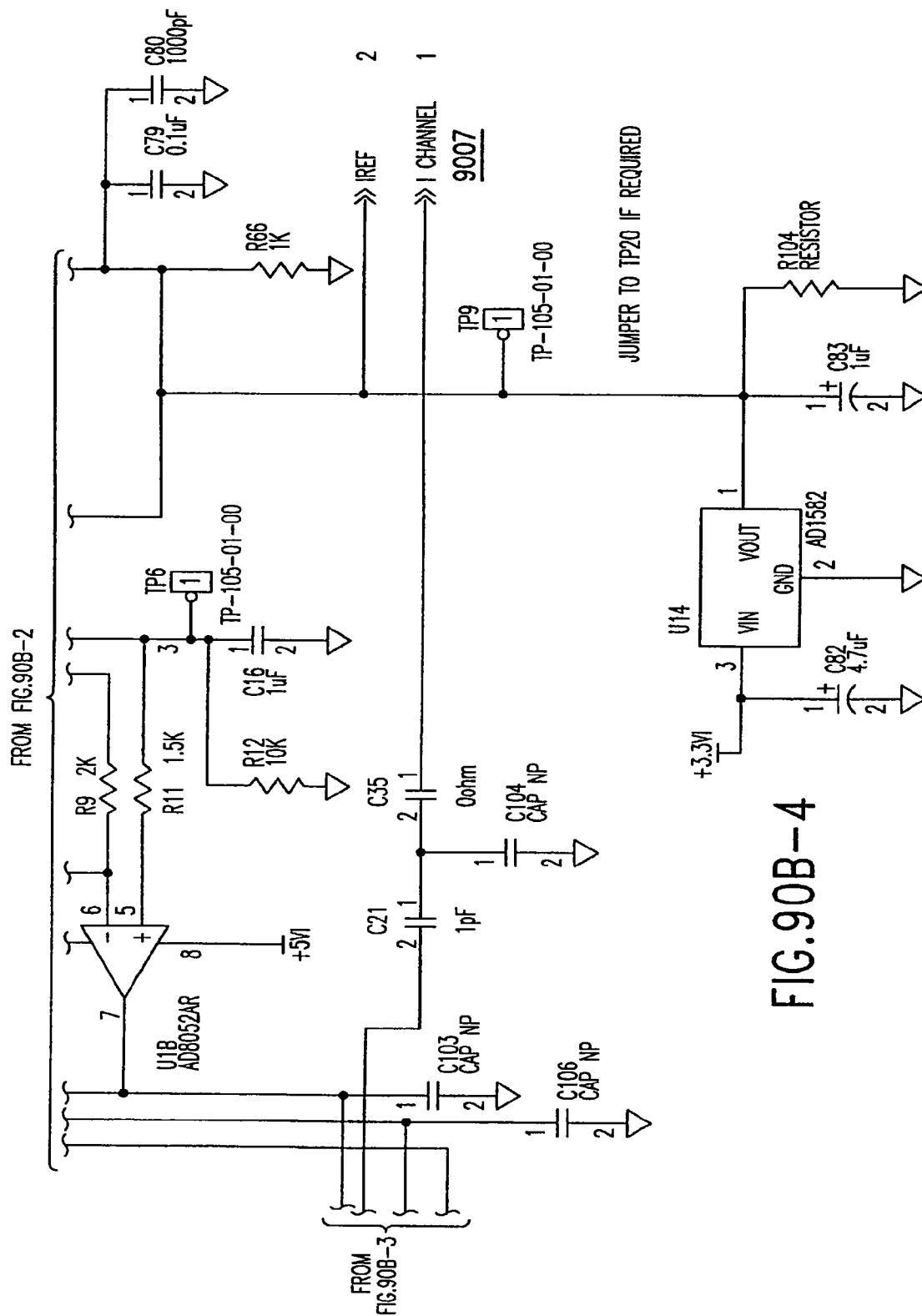


FIG. 90B-3



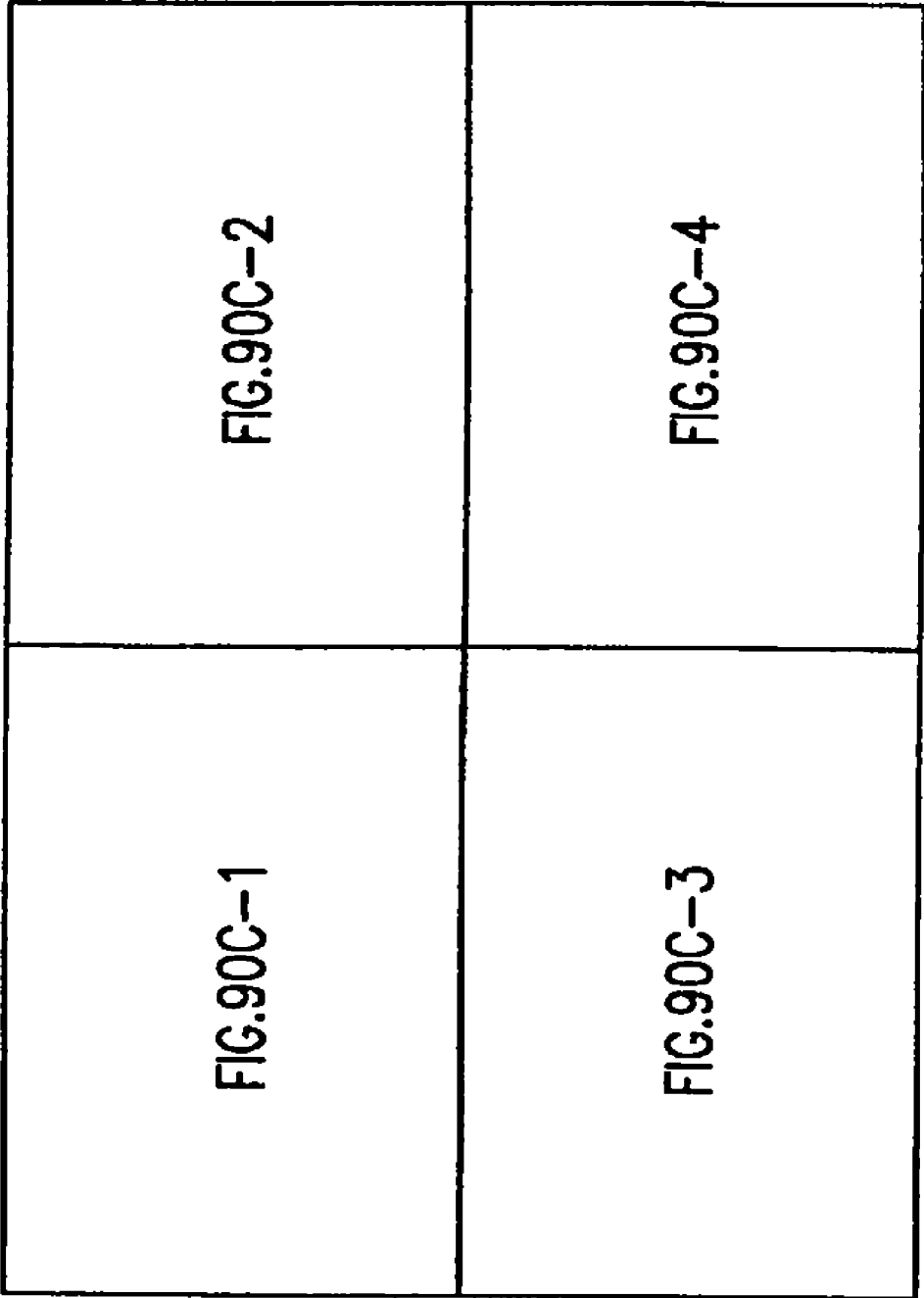


FIG.90C

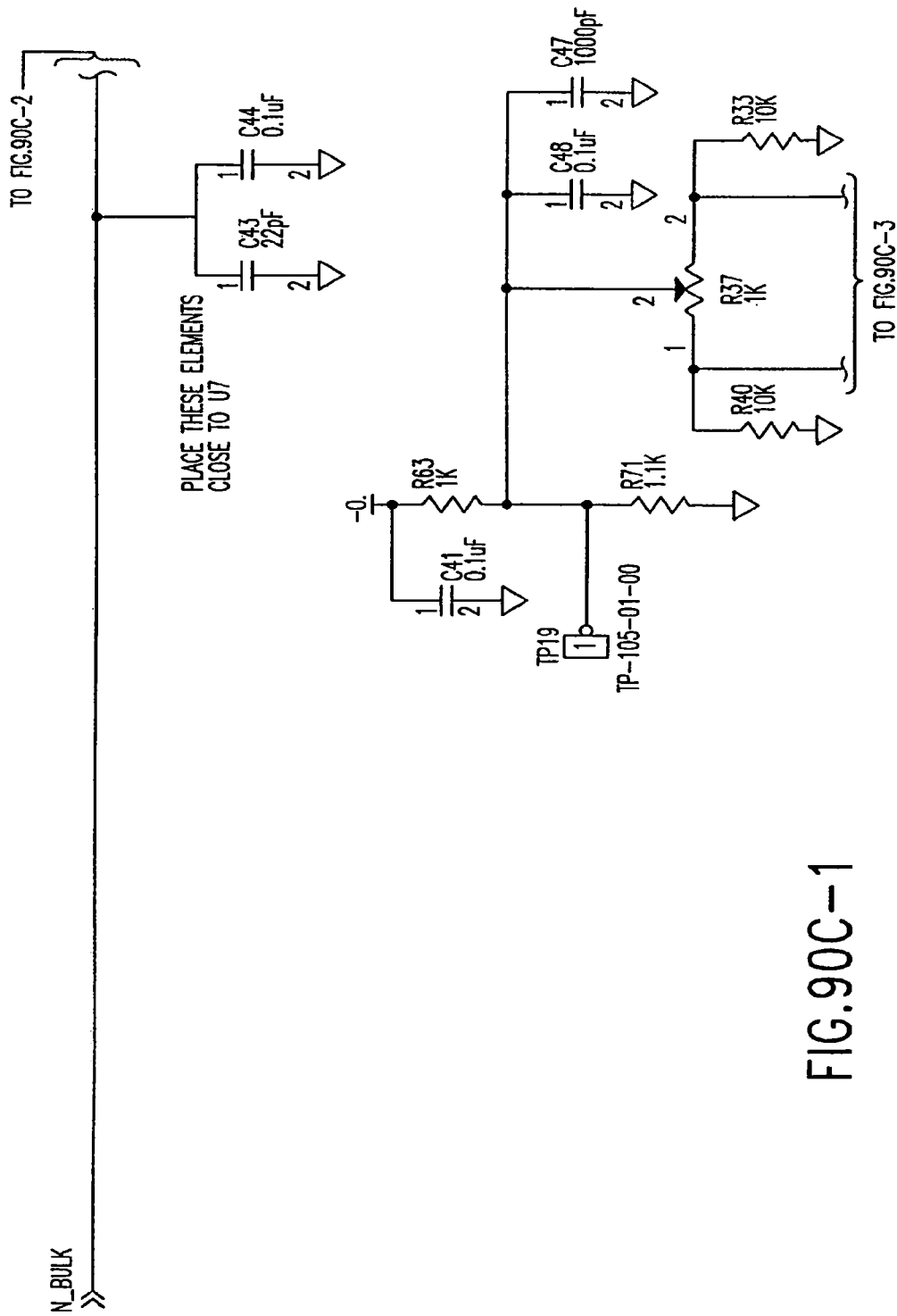
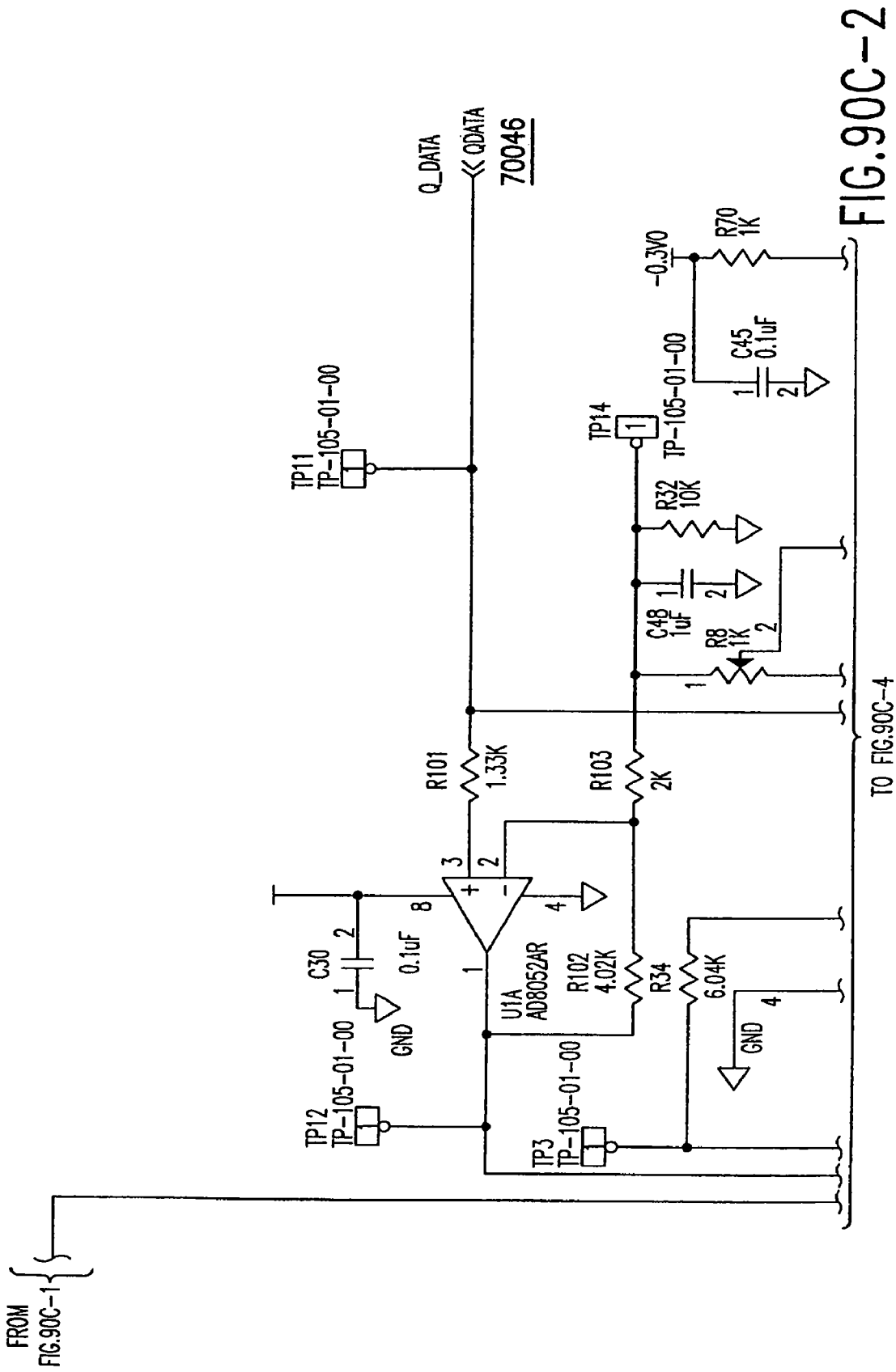


FIG. 90C-1



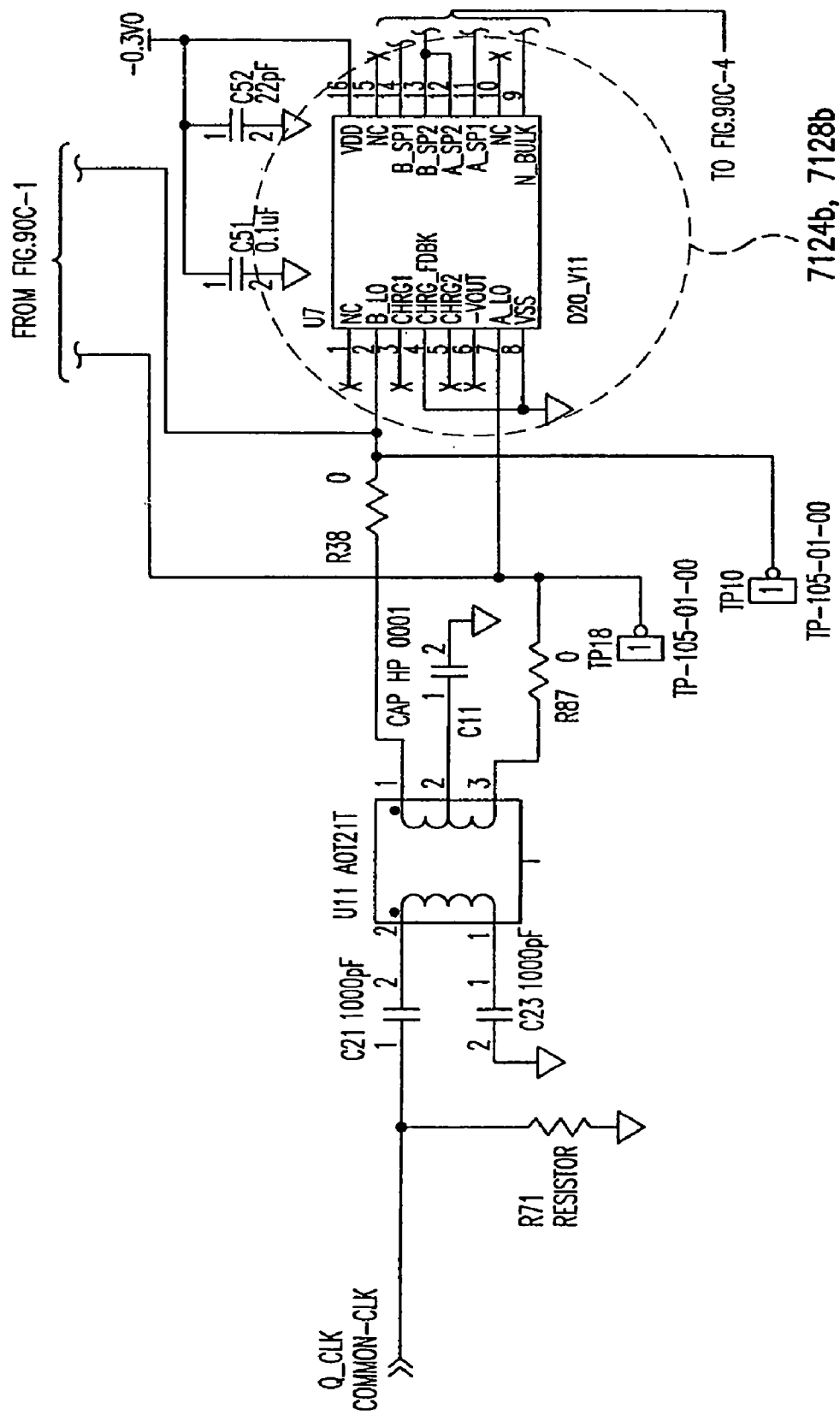
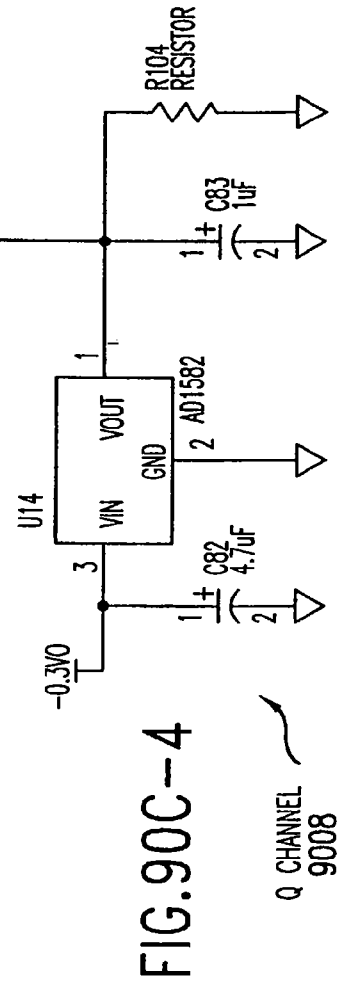
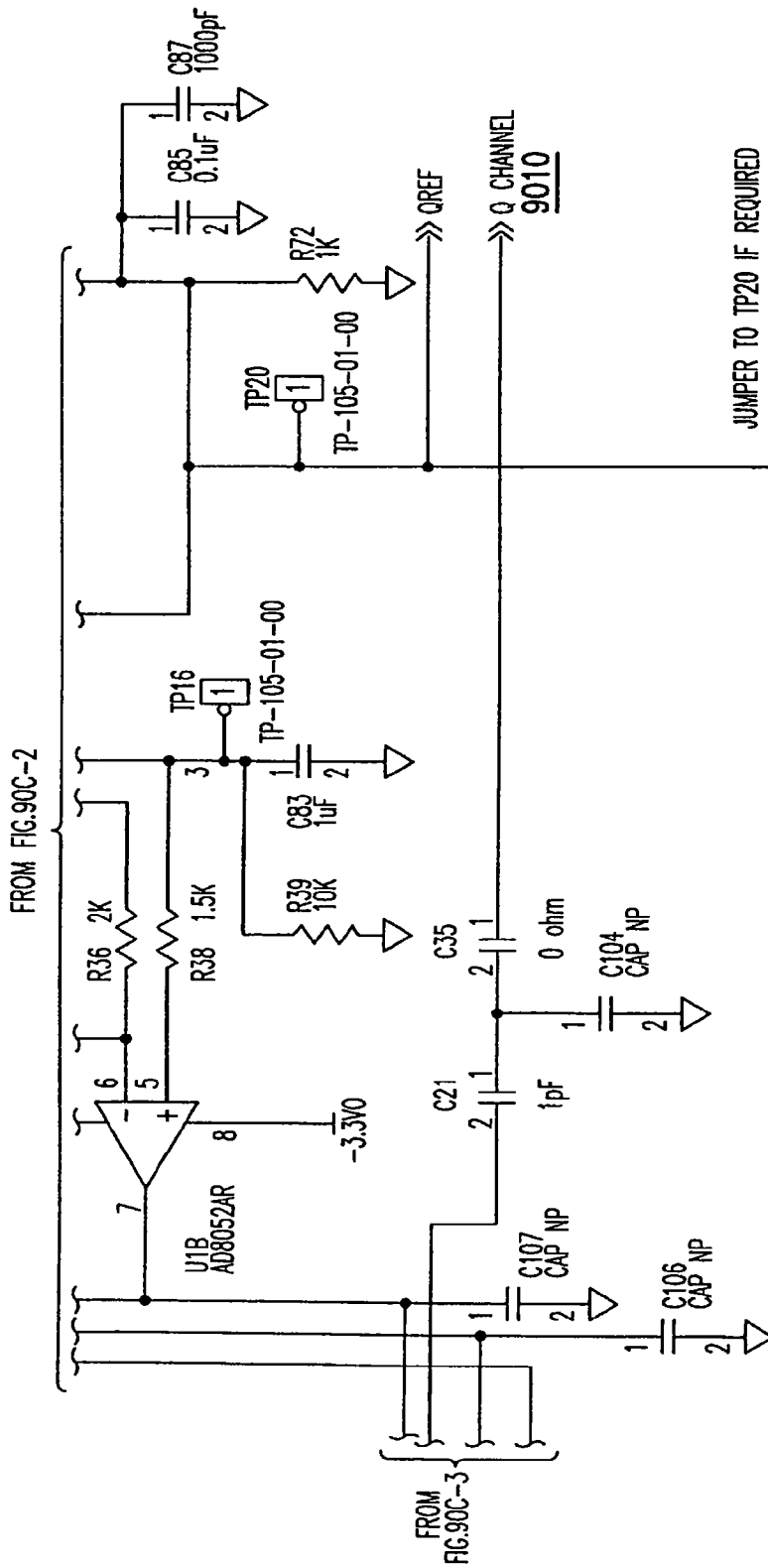
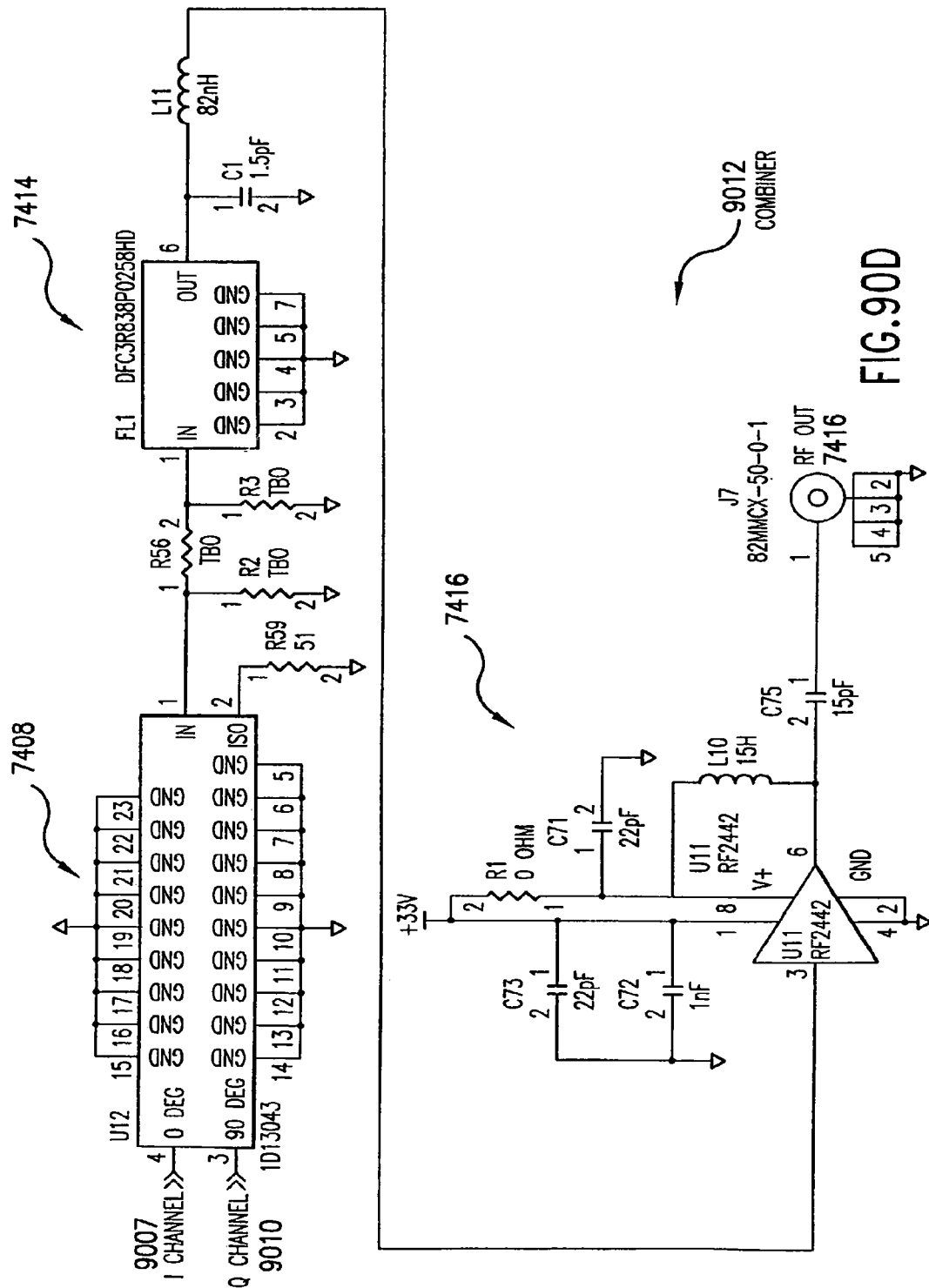


FIG. 90C-3







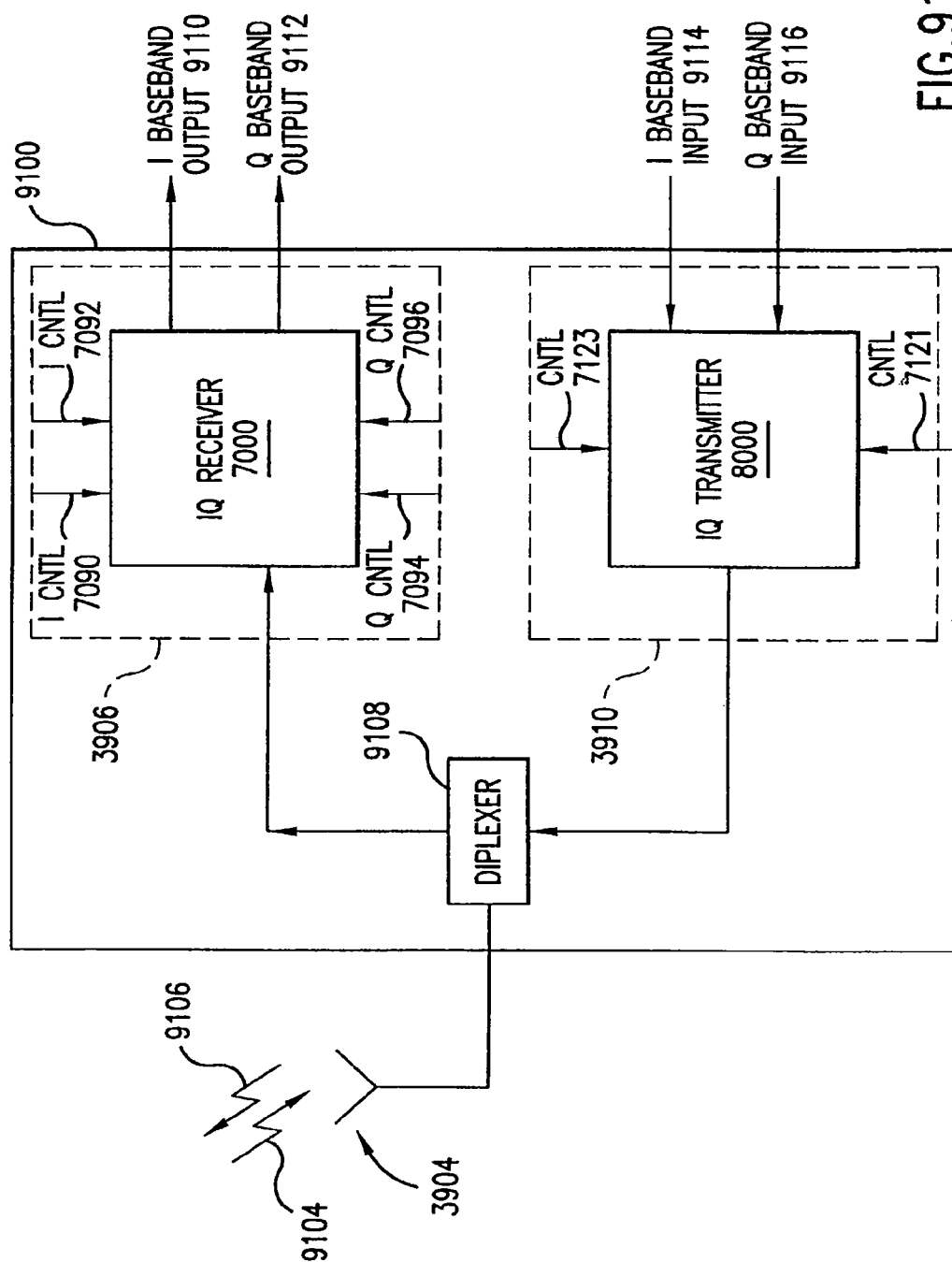


FIG. 91

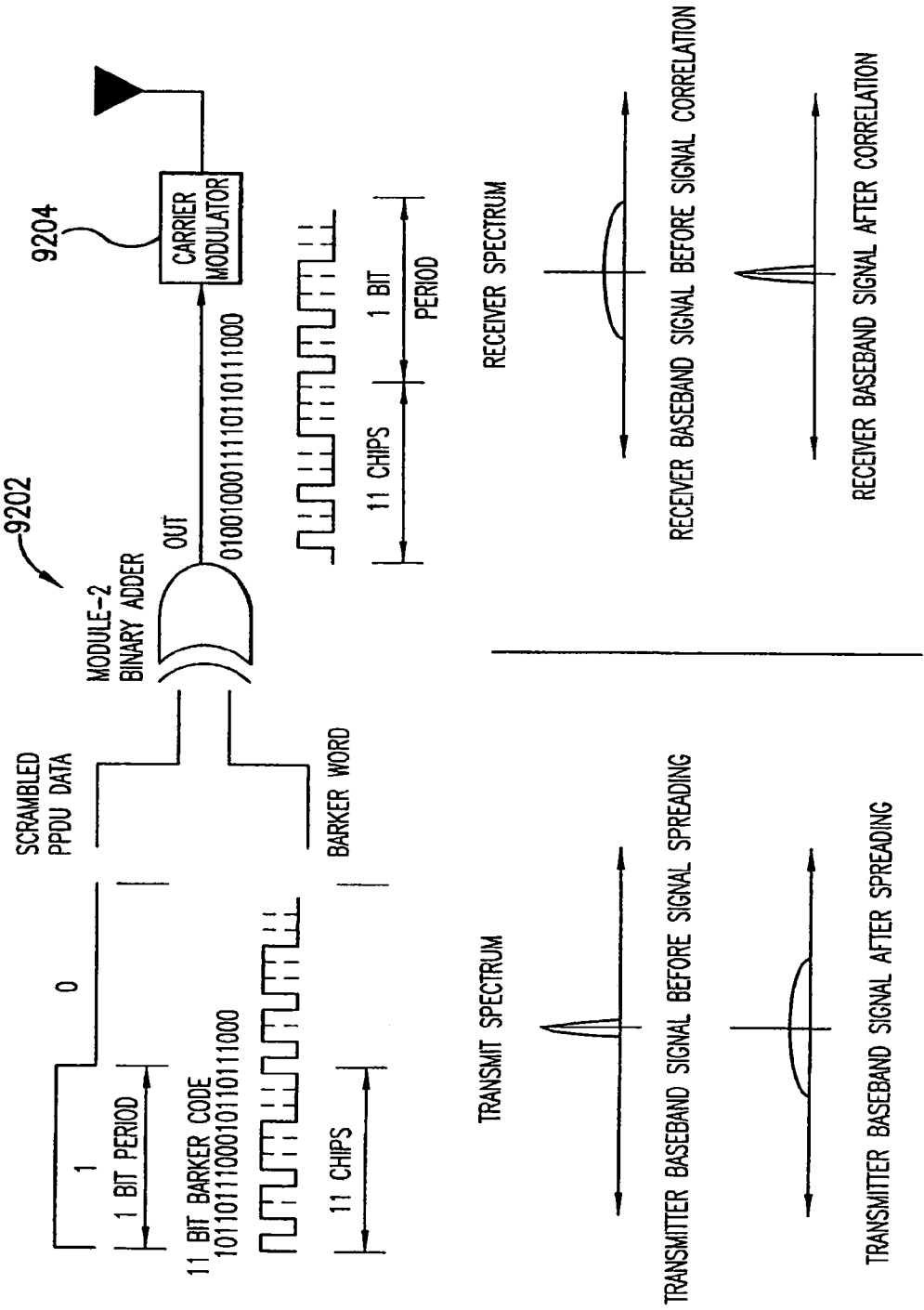


FIG.92

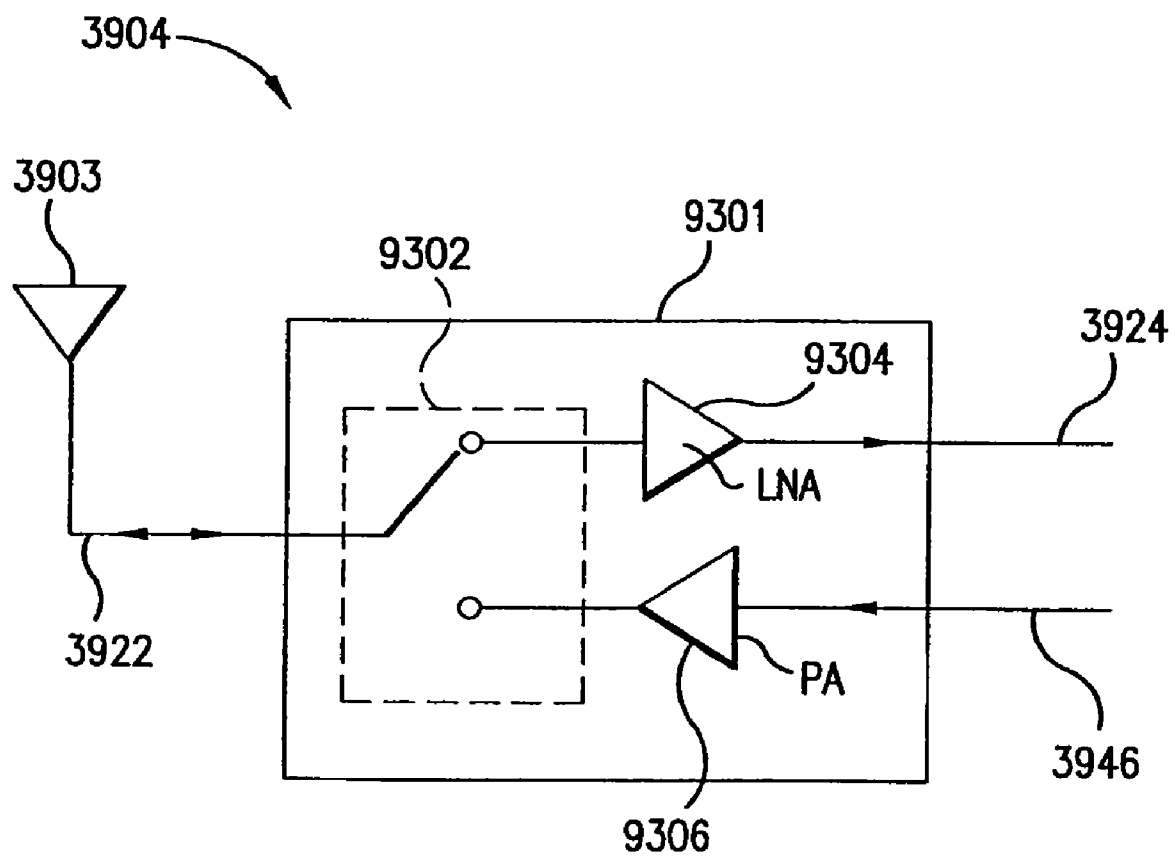


FIG.93

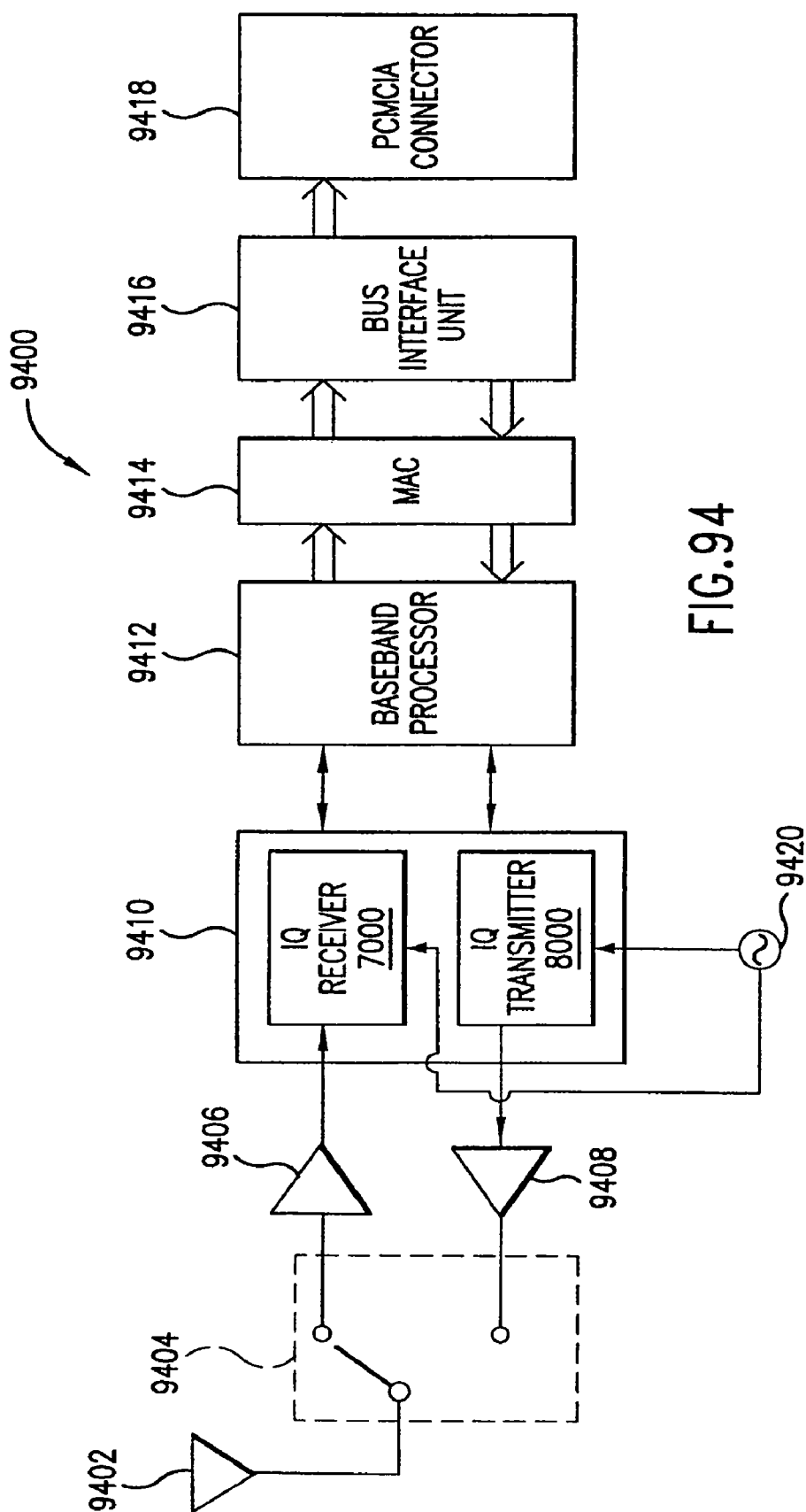


FIG. 94

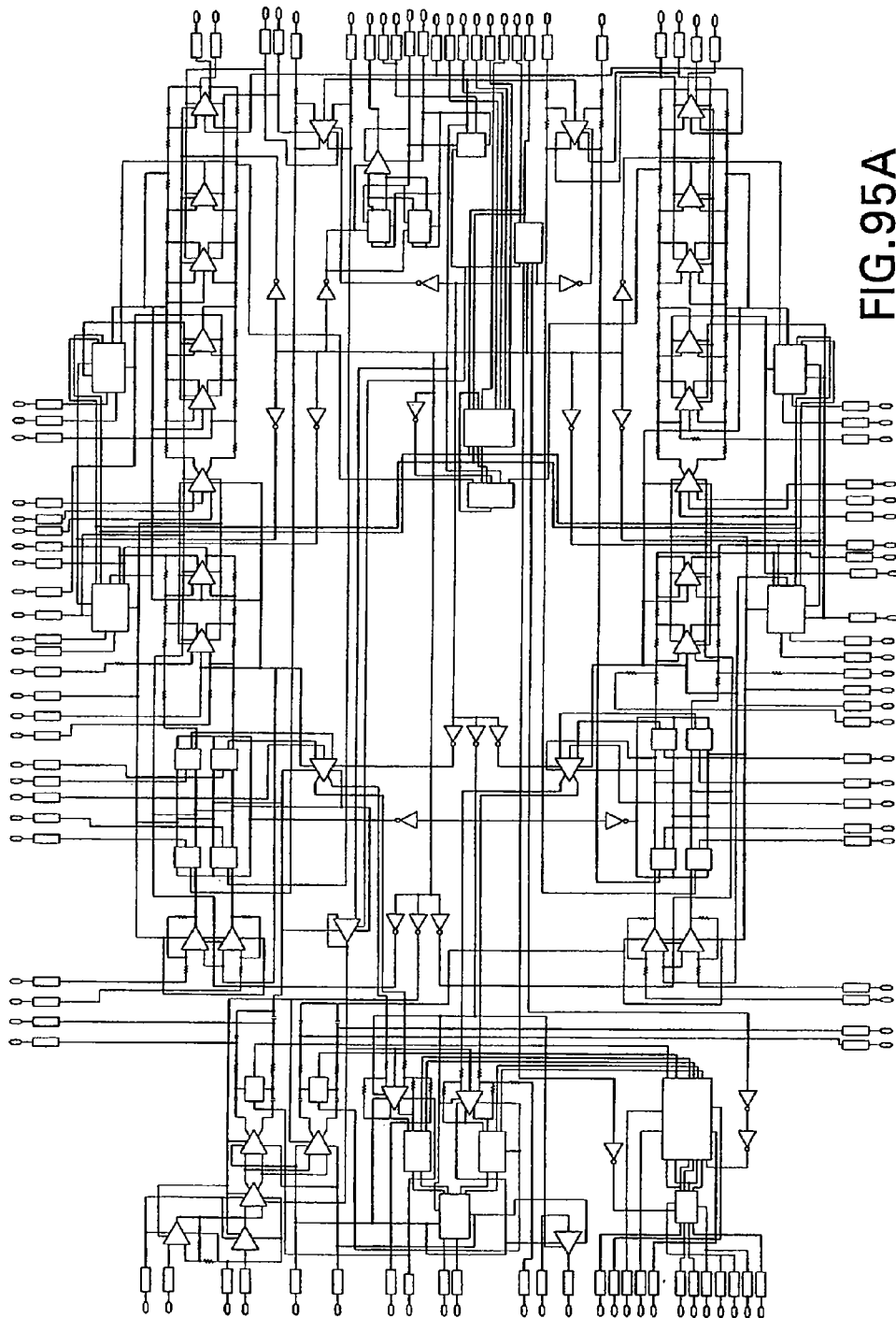


FIG. 95A

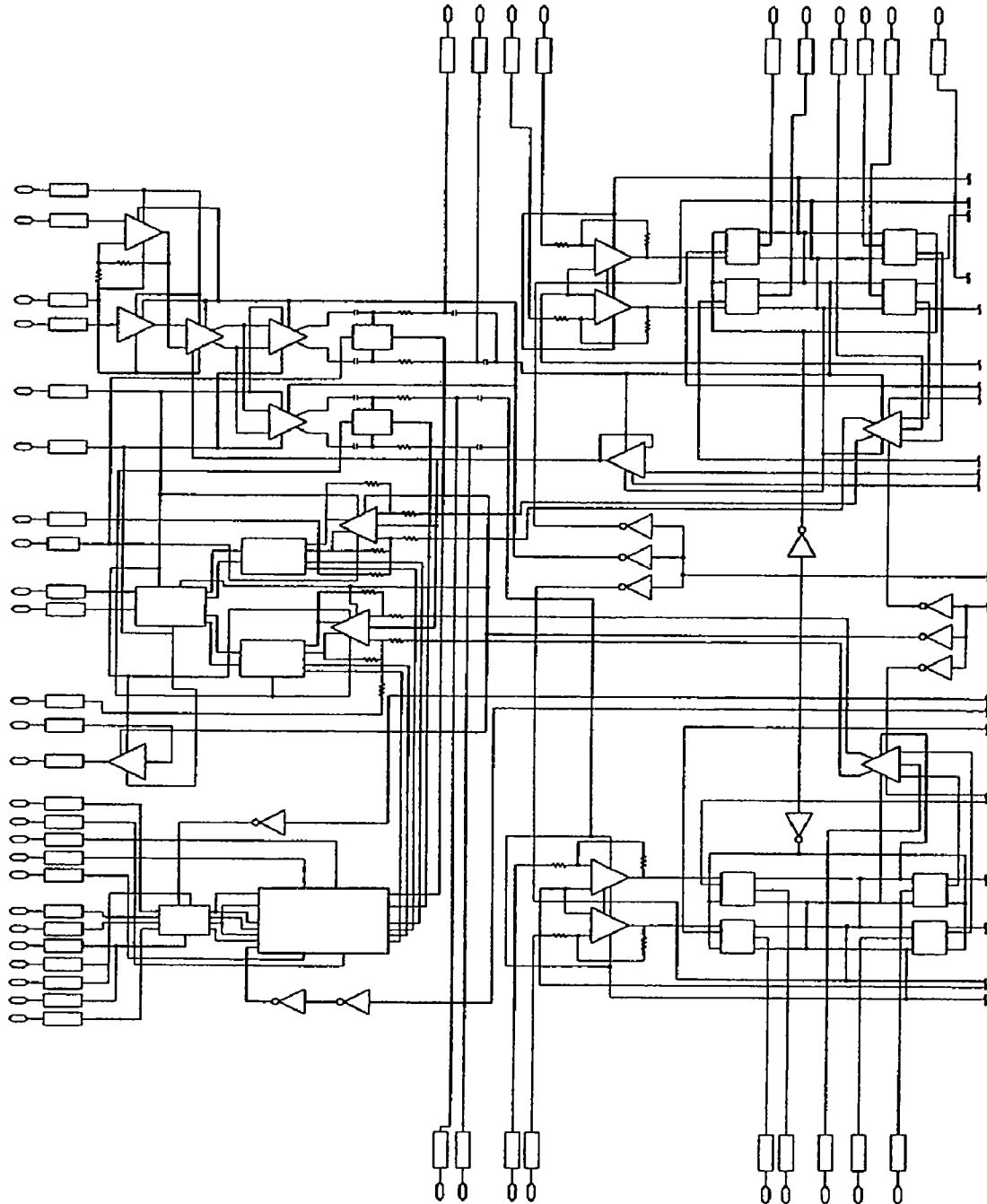


FIG. 95B



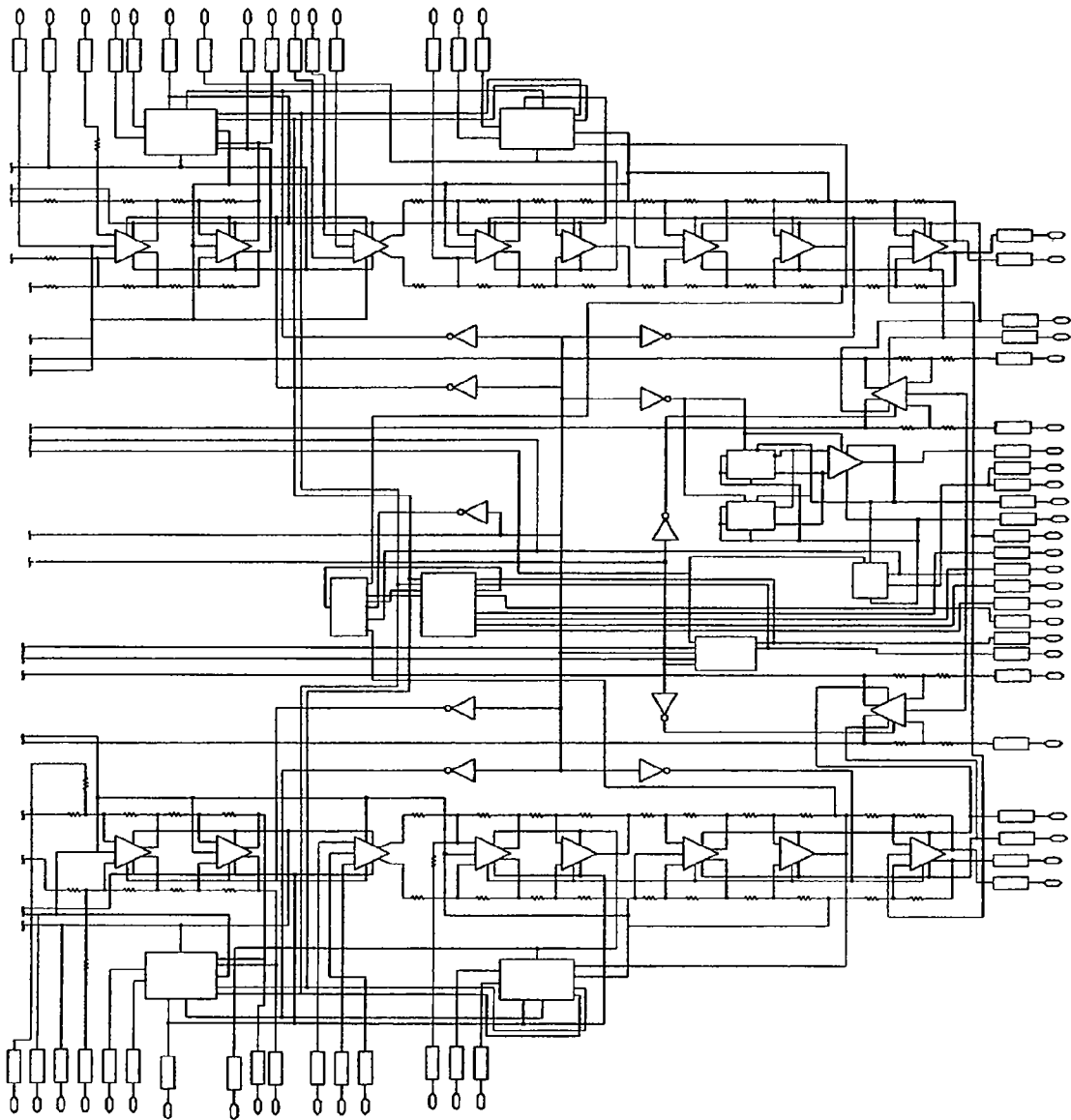


FIG. 95C

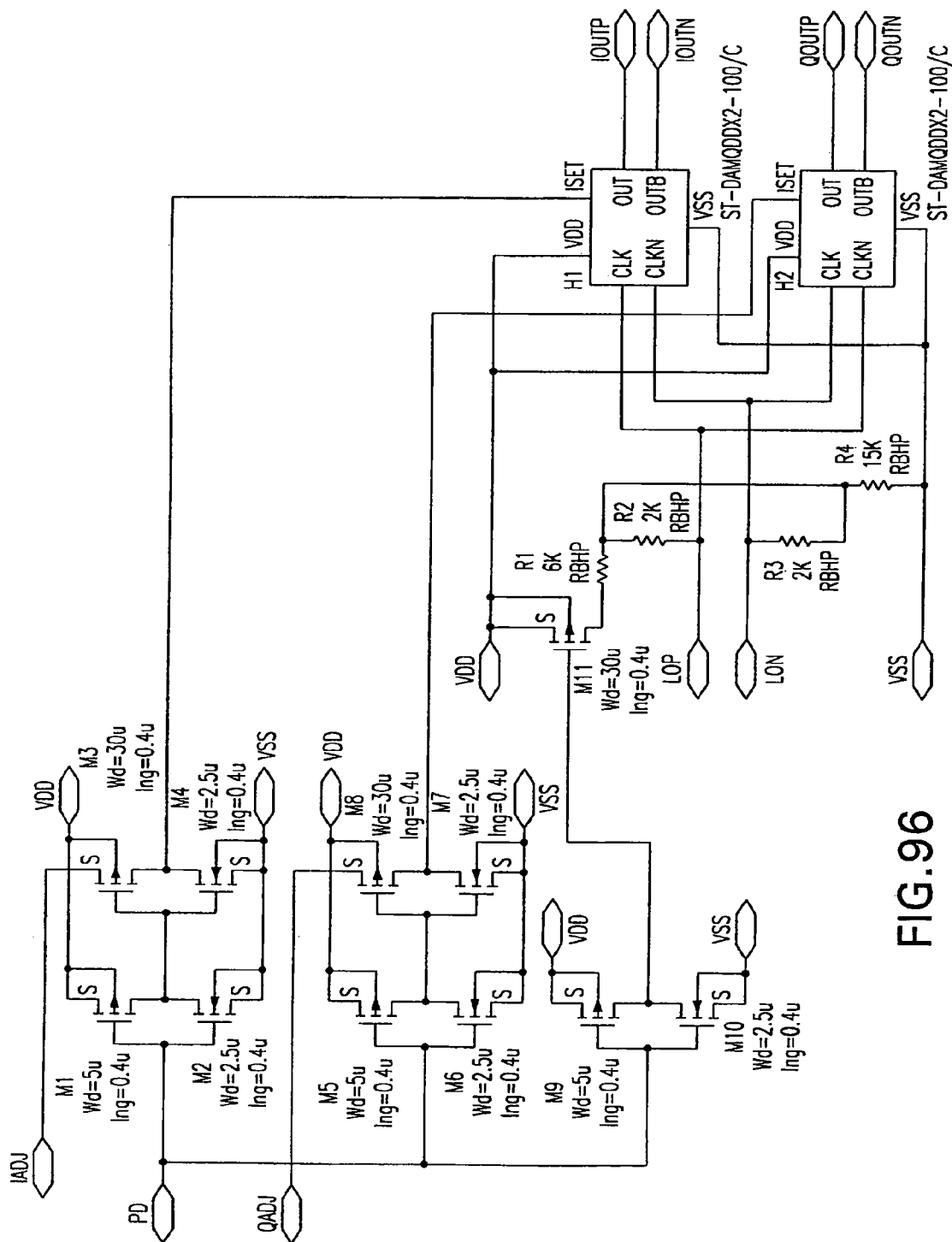


FIG. 96

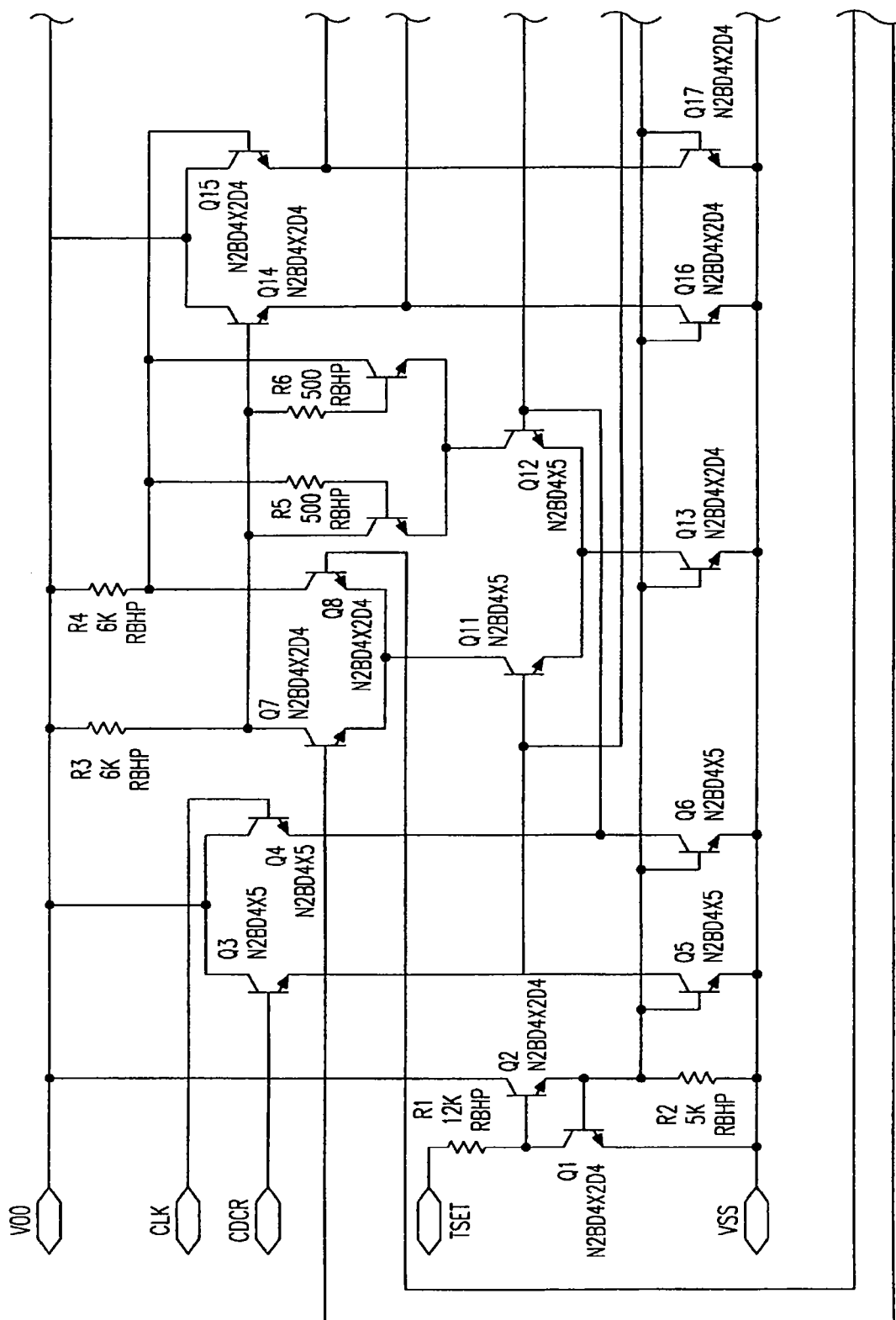


FIG. 97A

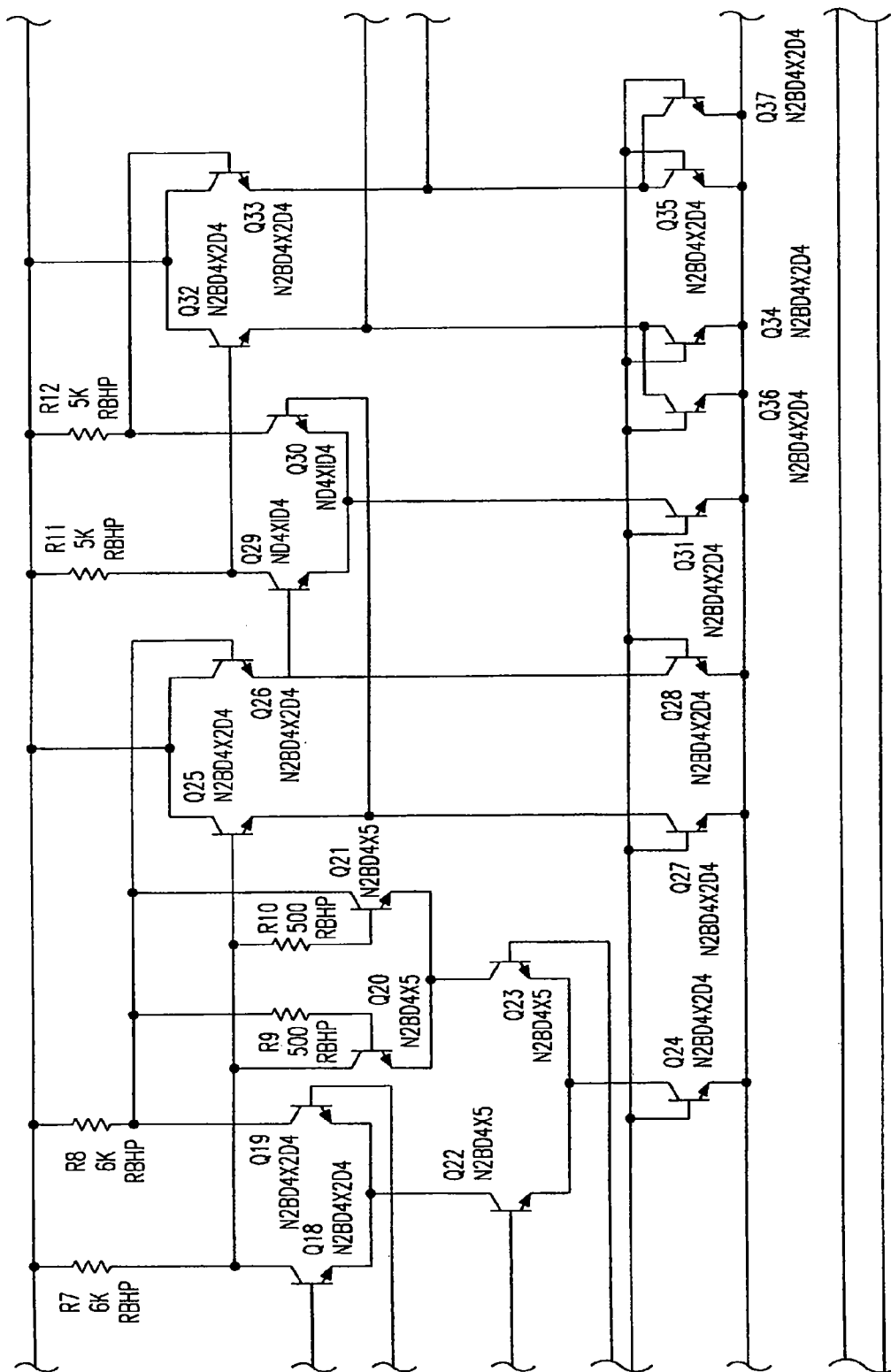


FIG. 97B

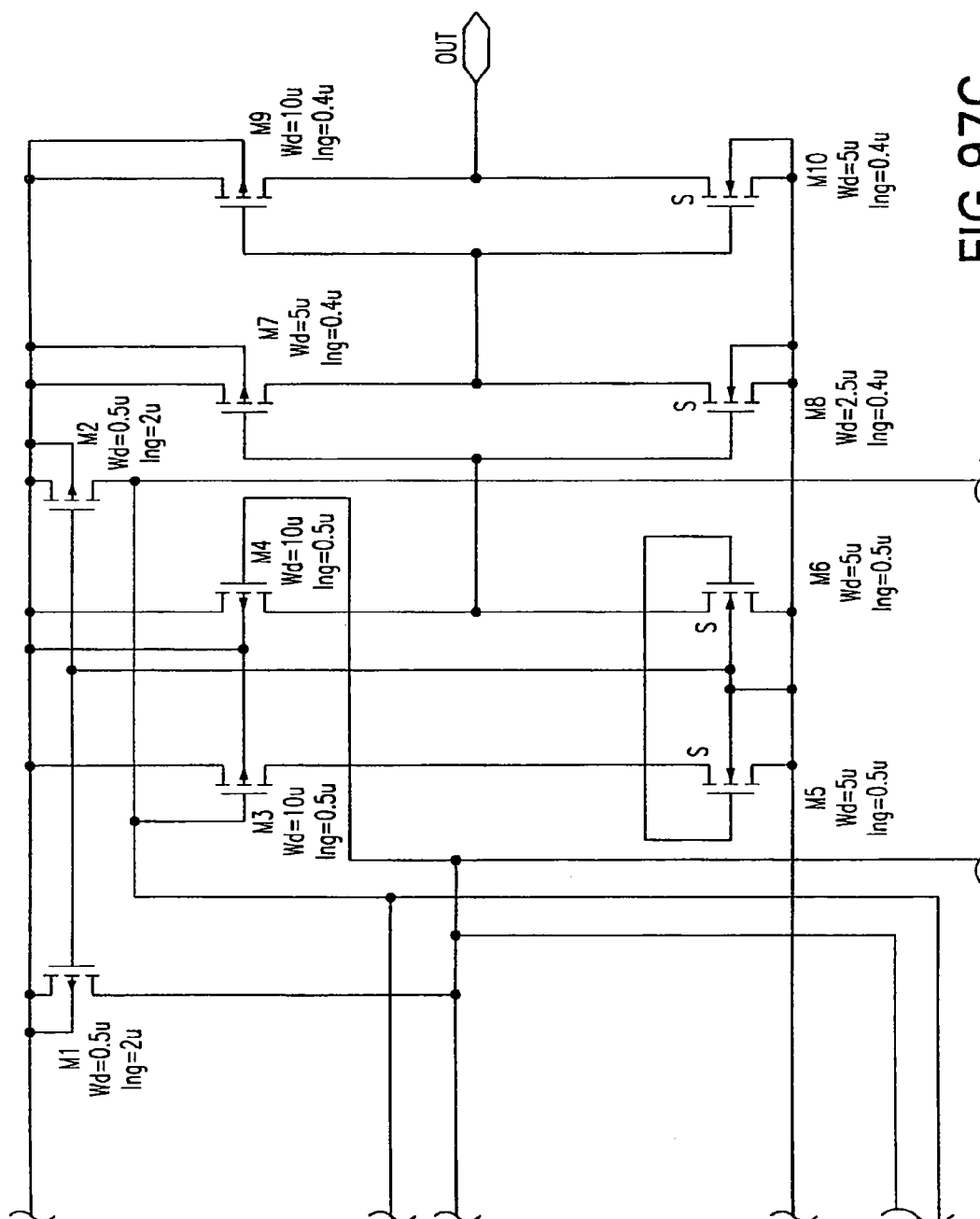


FIG. 97C

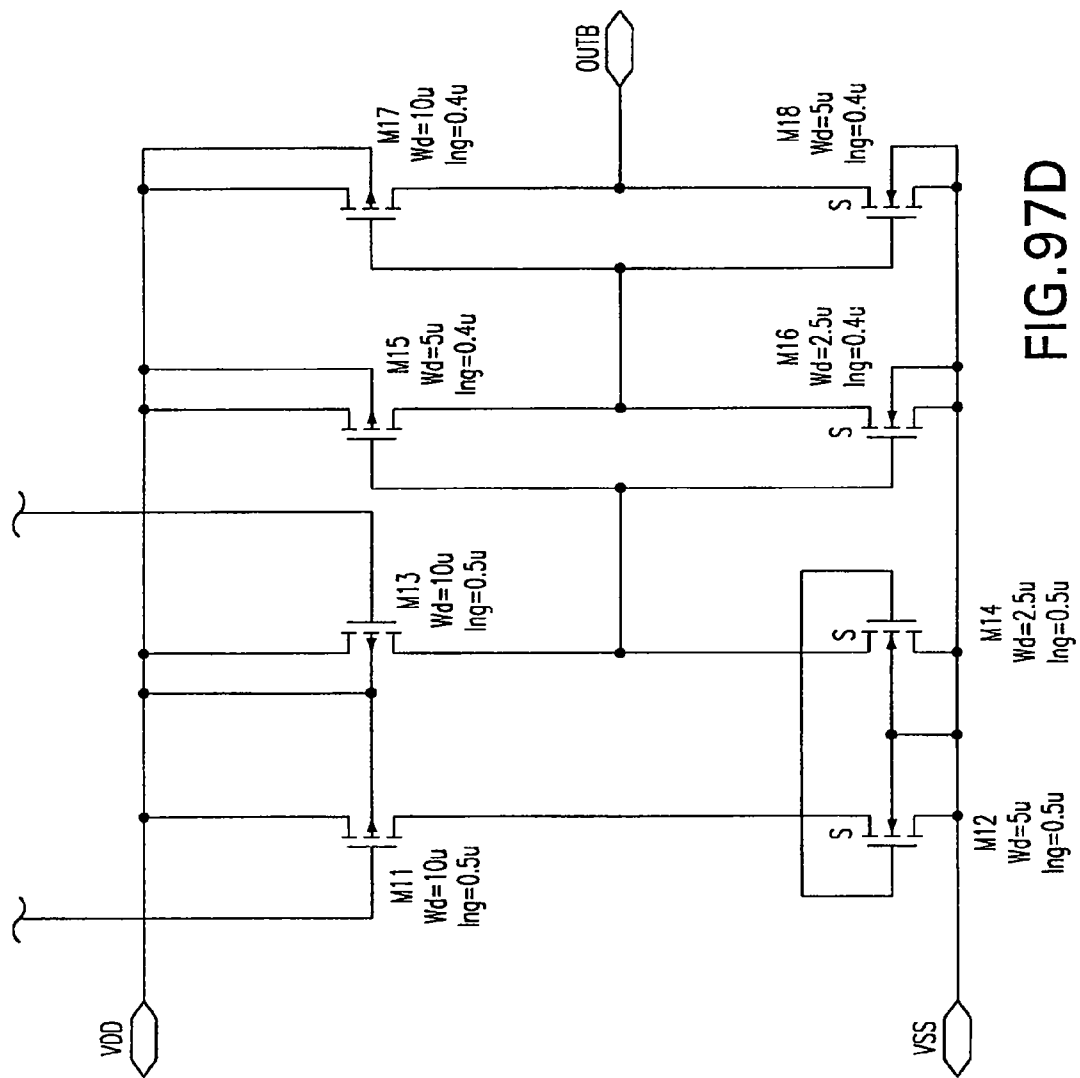


FIG. 97D

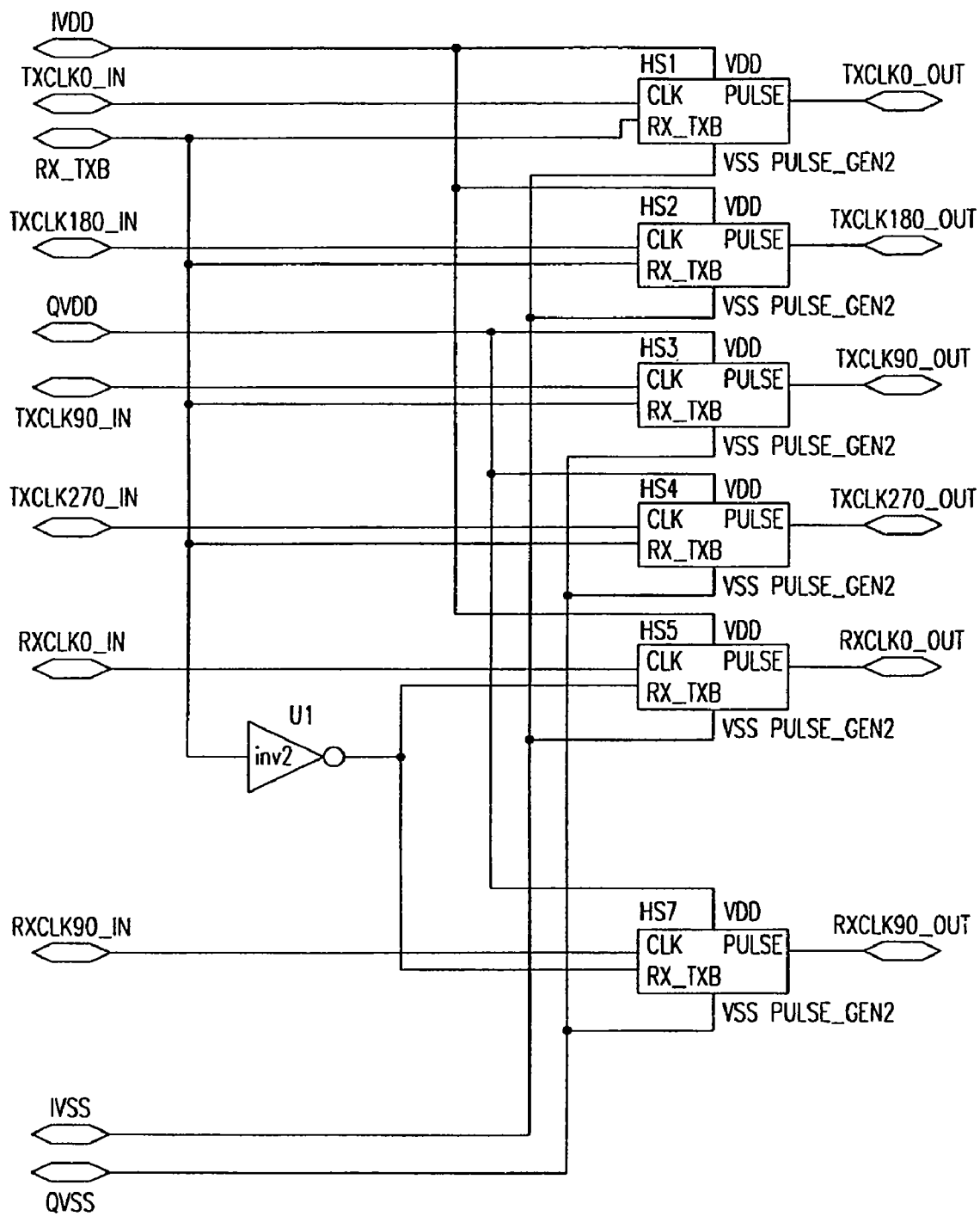


FIG. 98

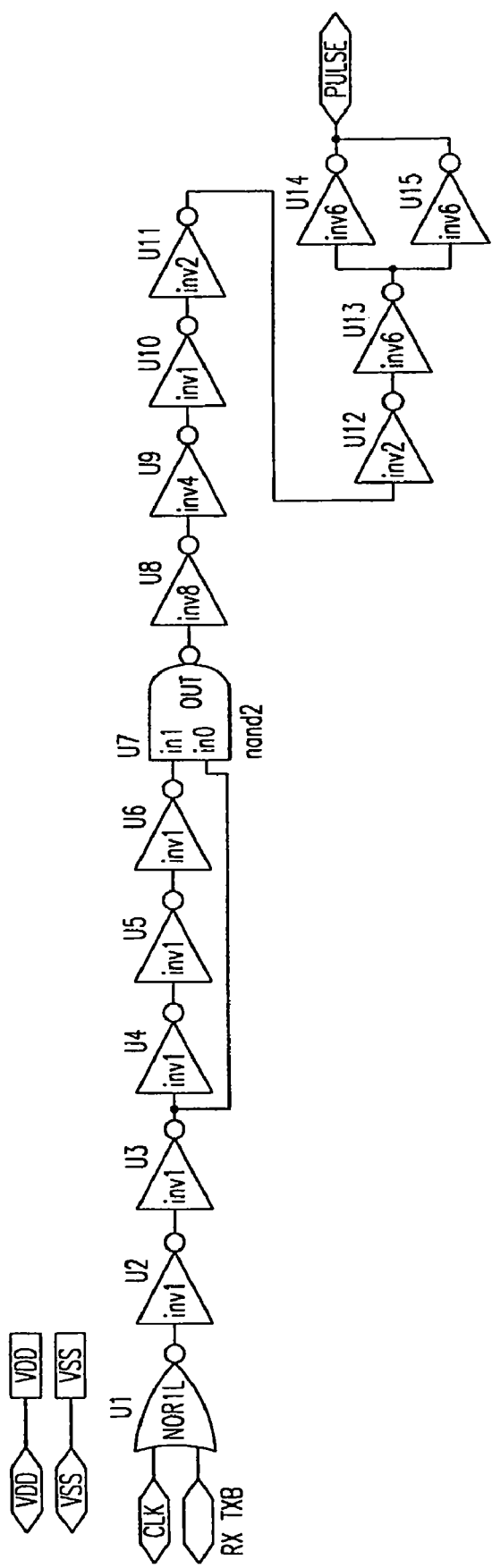


FIG. 99



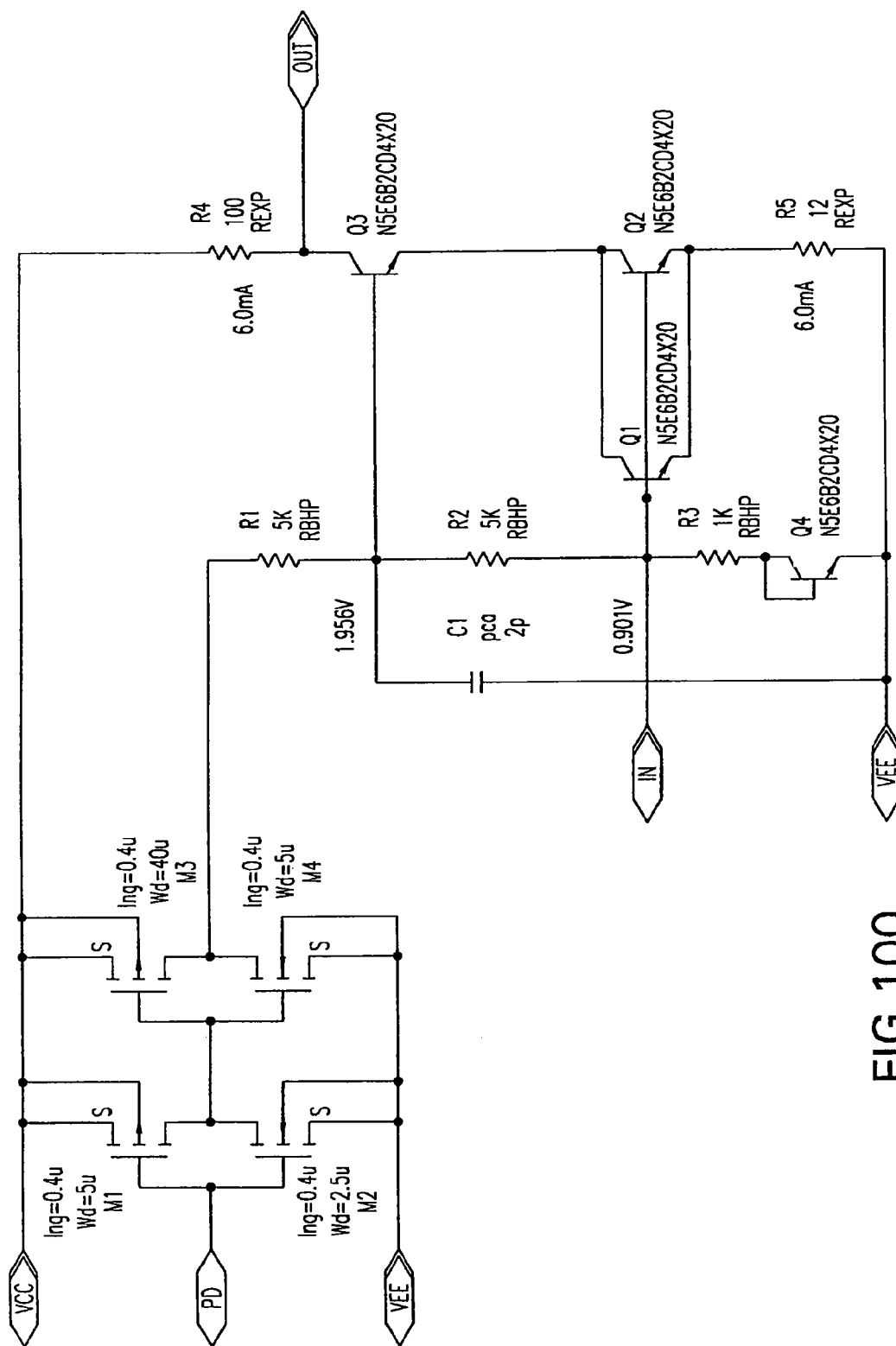


FIG. 100

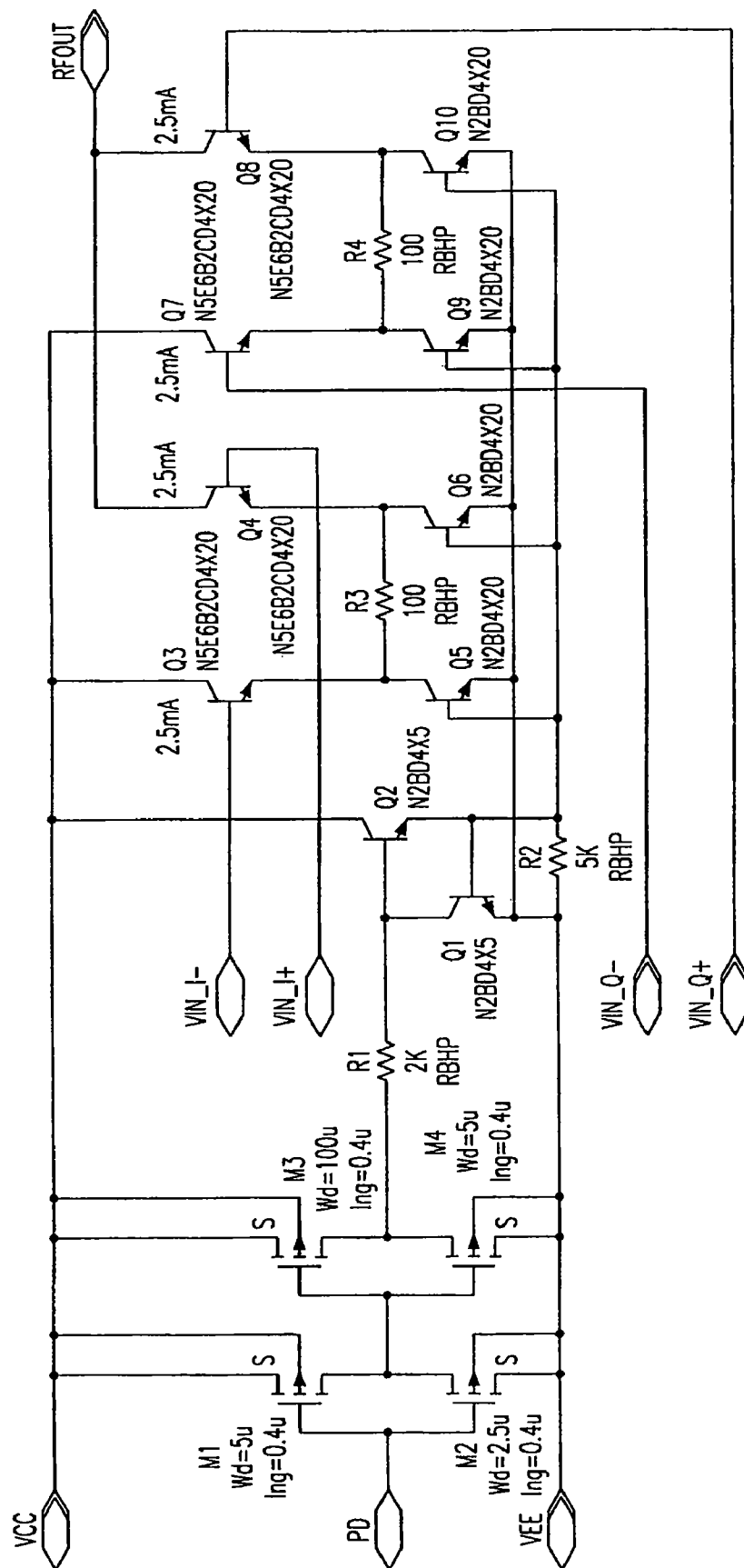


FIG. 101

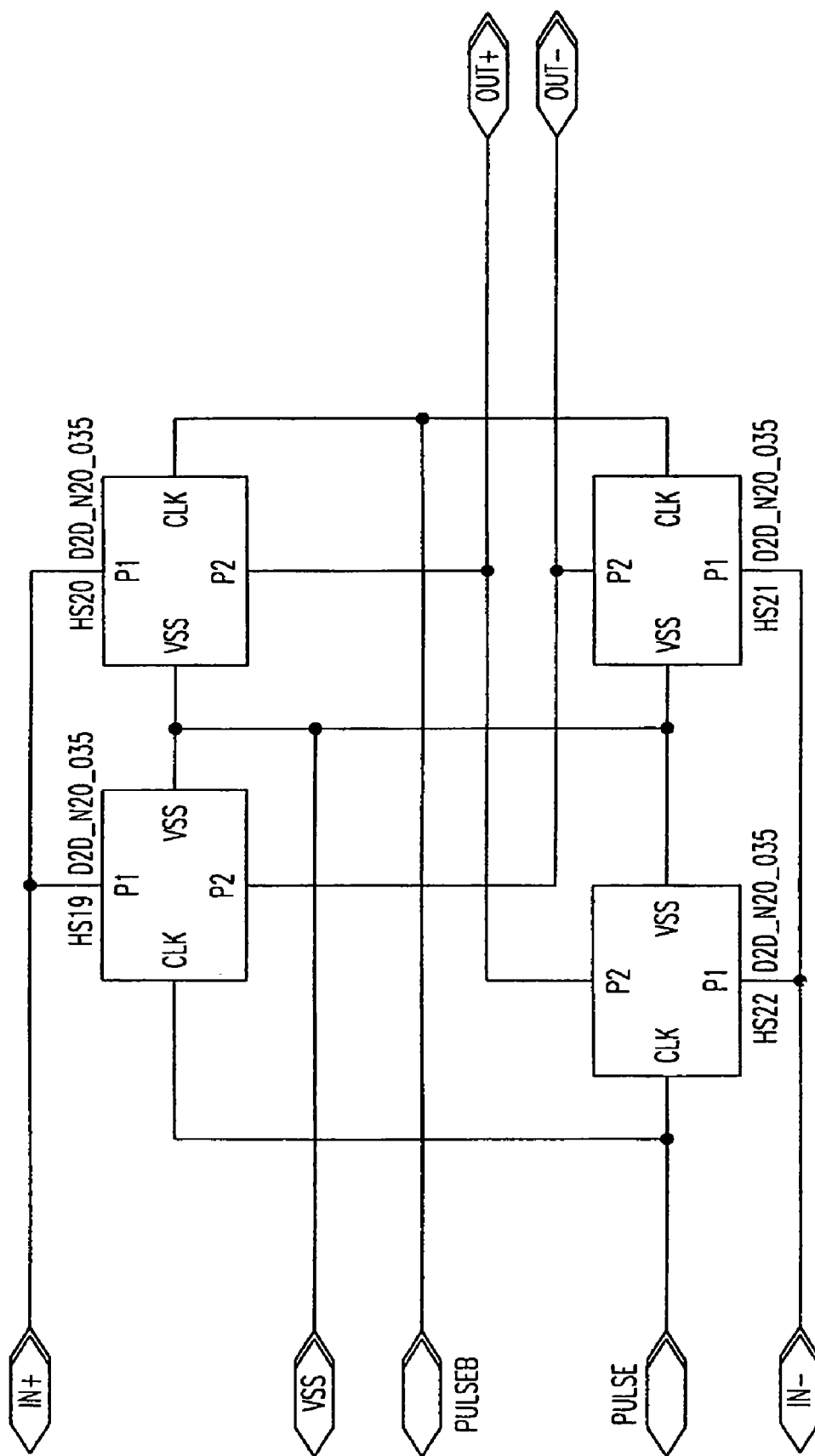
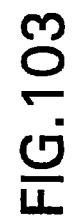


FIG. 102



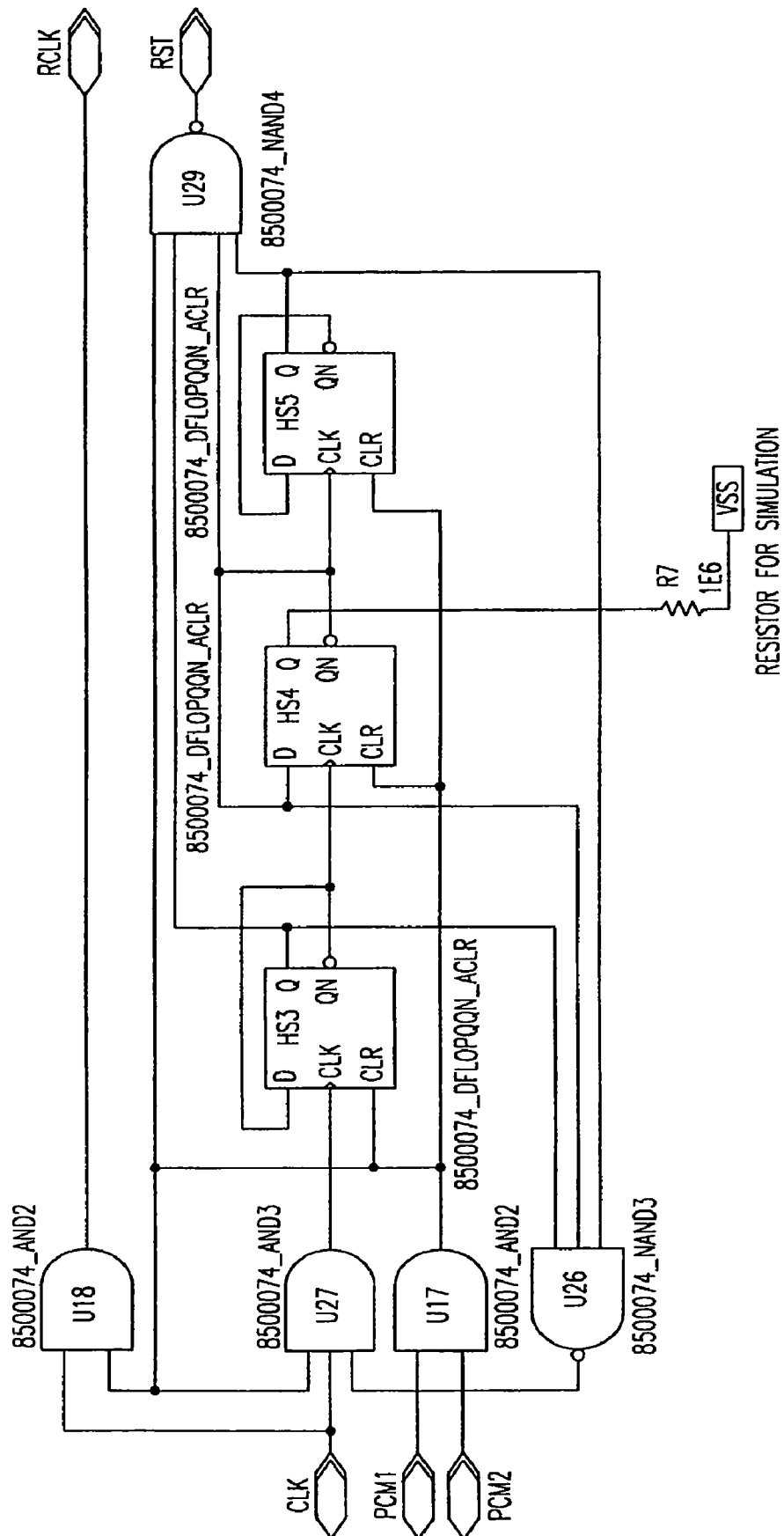


FIG. 104

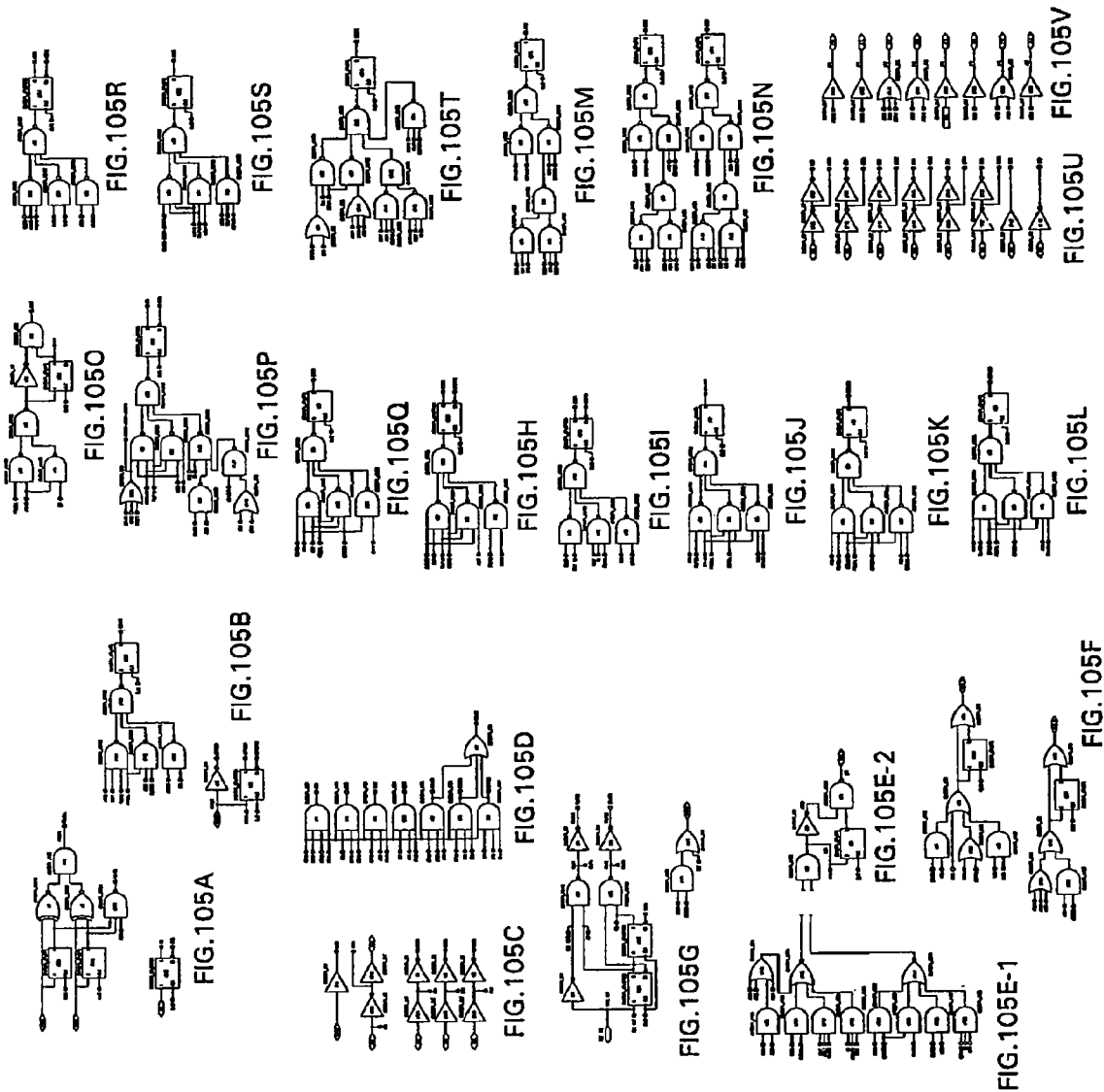


FIG. 105

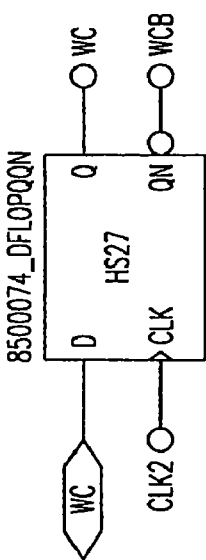
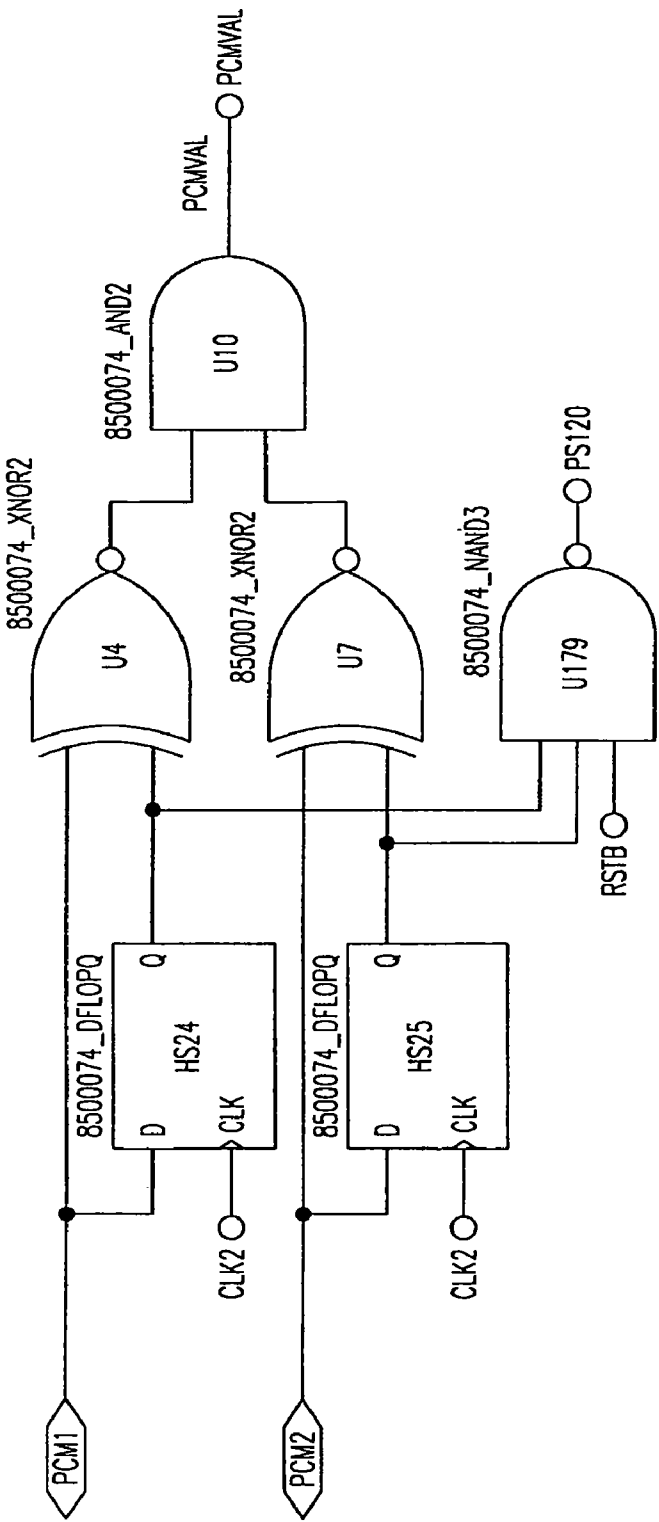
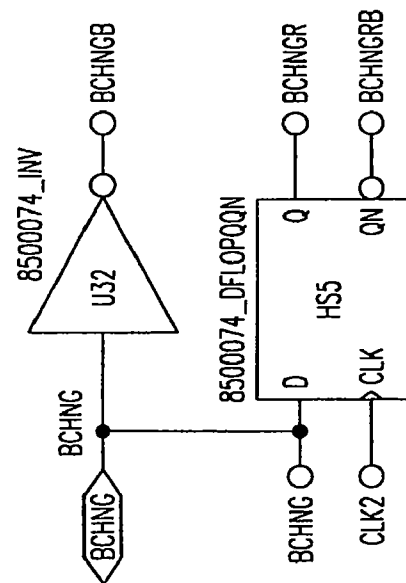
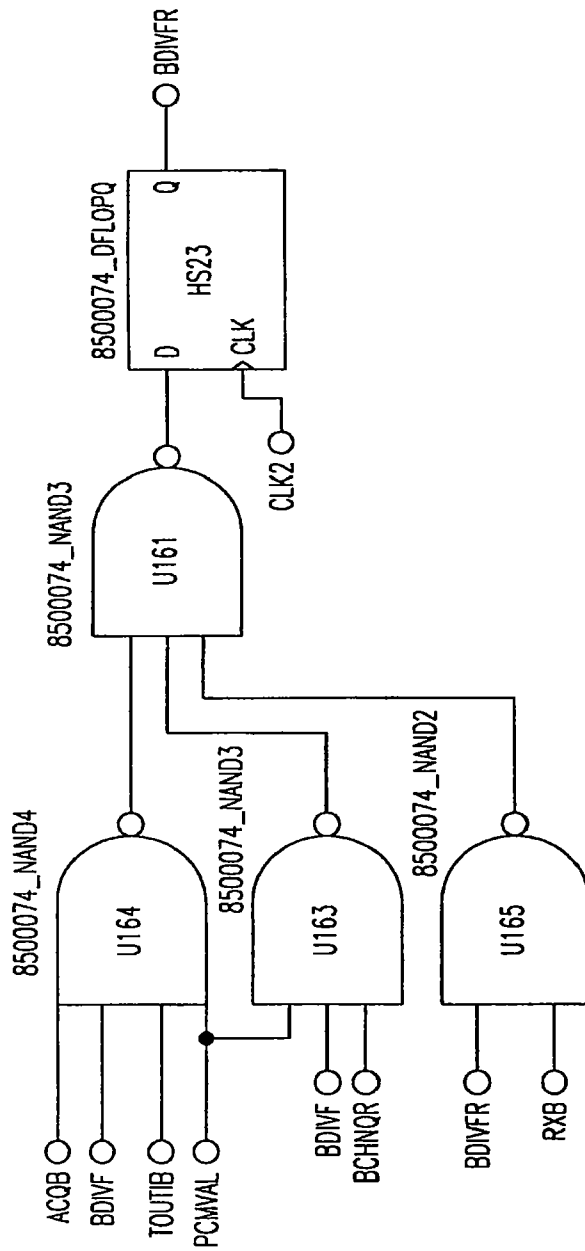


FIG. 105A



**FIG. 105B**



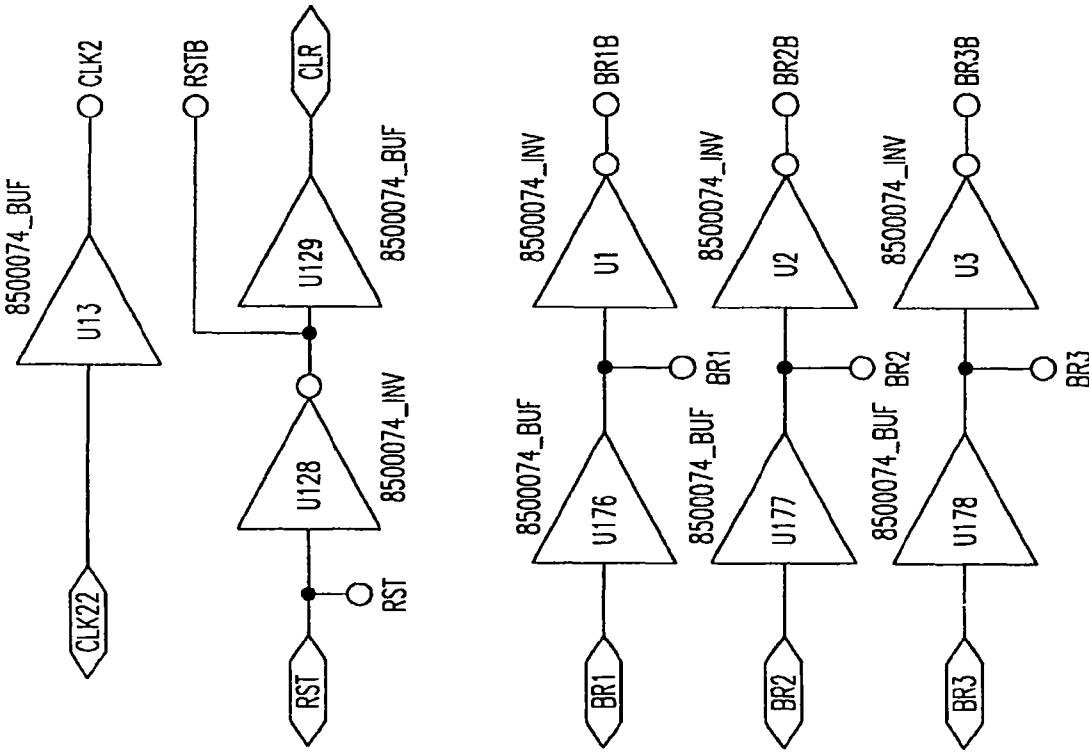


FIG. 105C

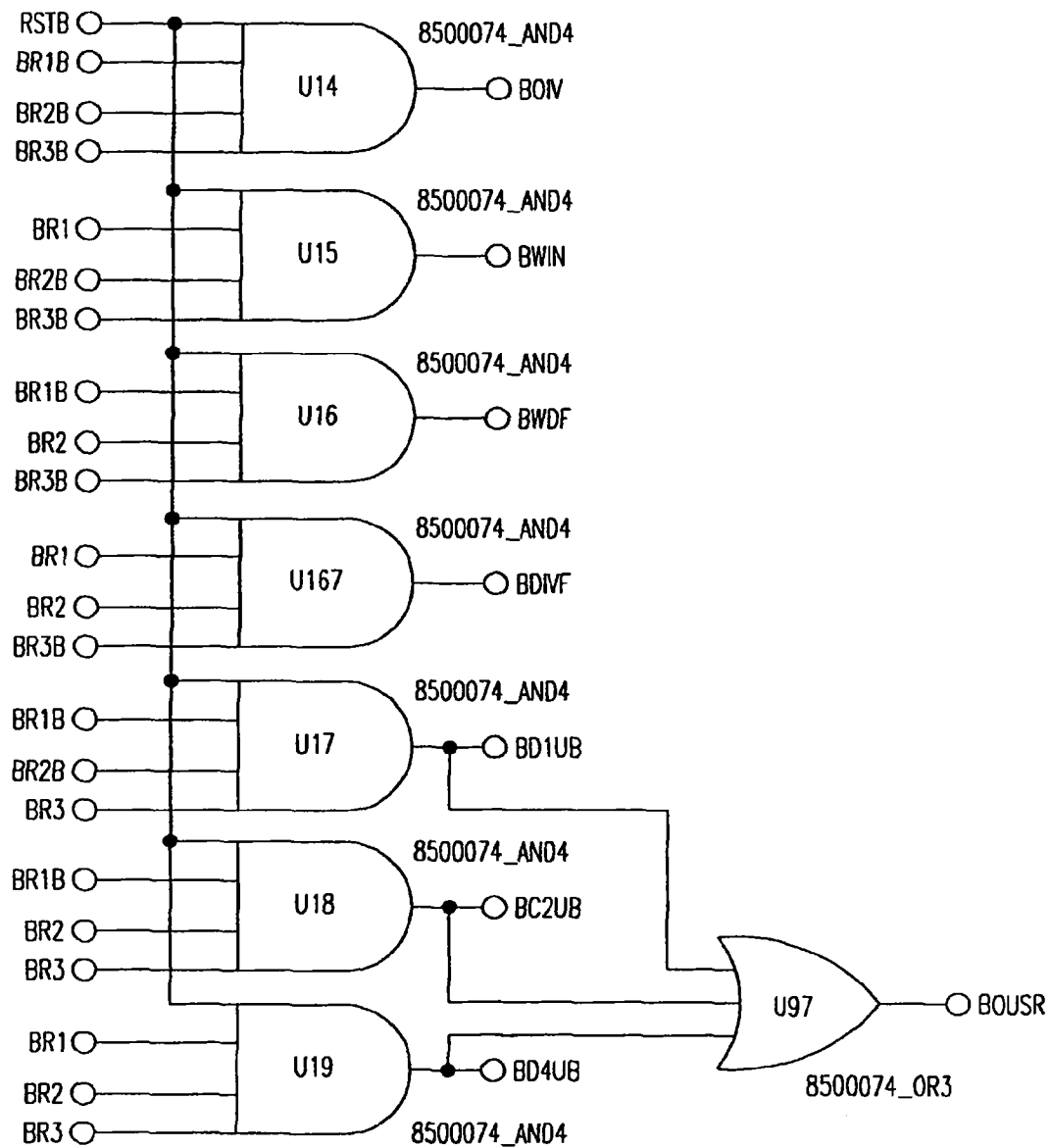


FIG. 105D

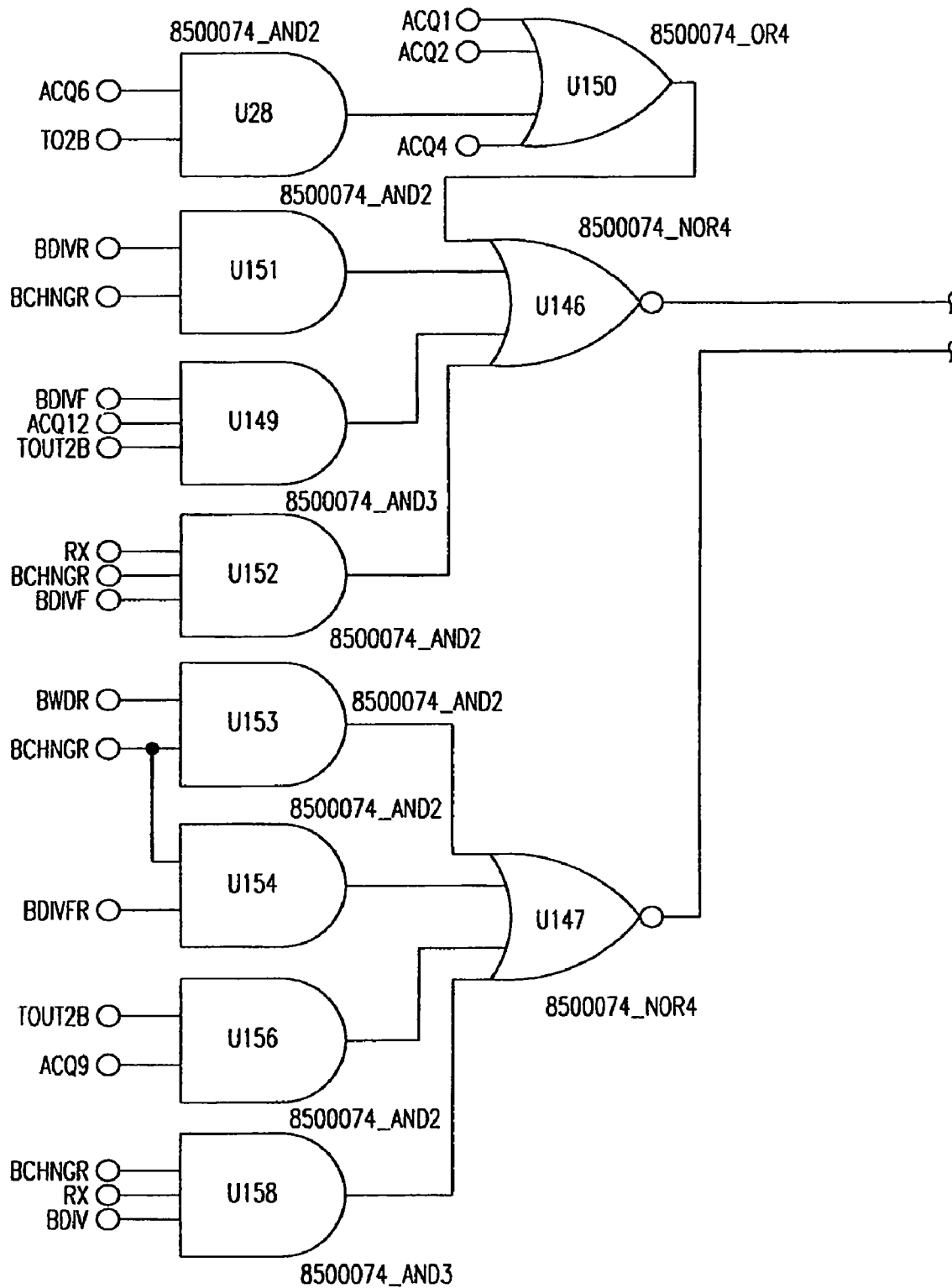


FIG. 105E-1

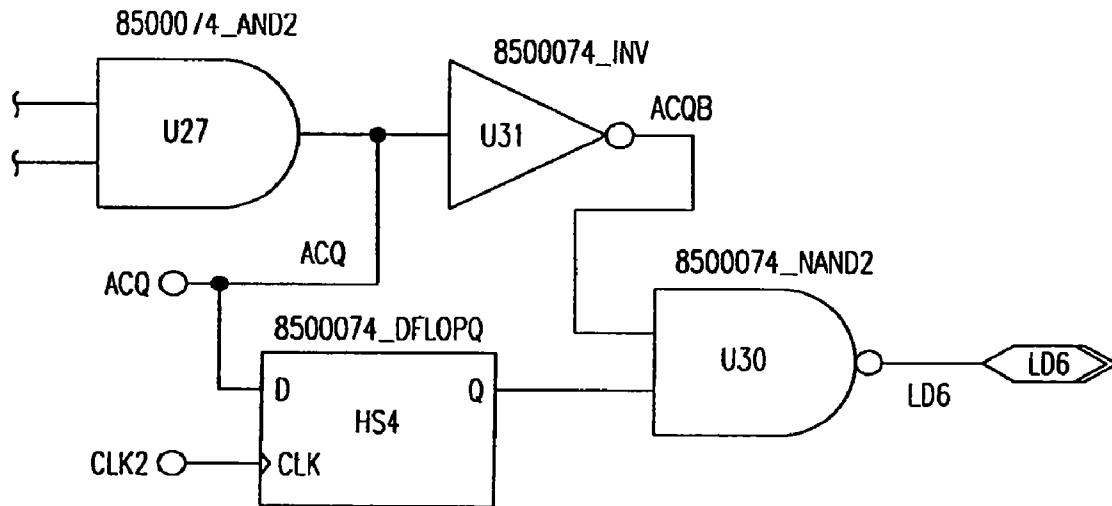


FIG. 105E-2

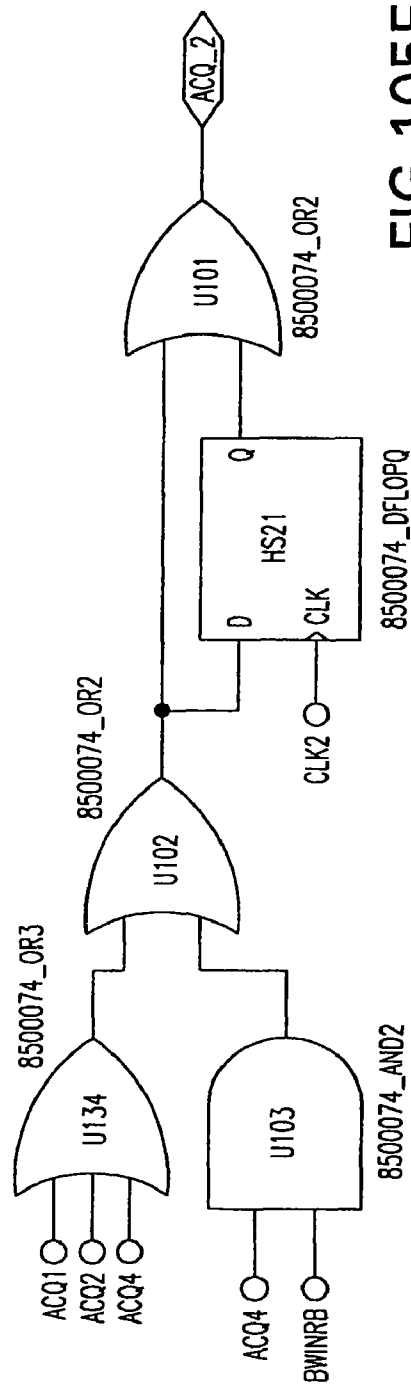
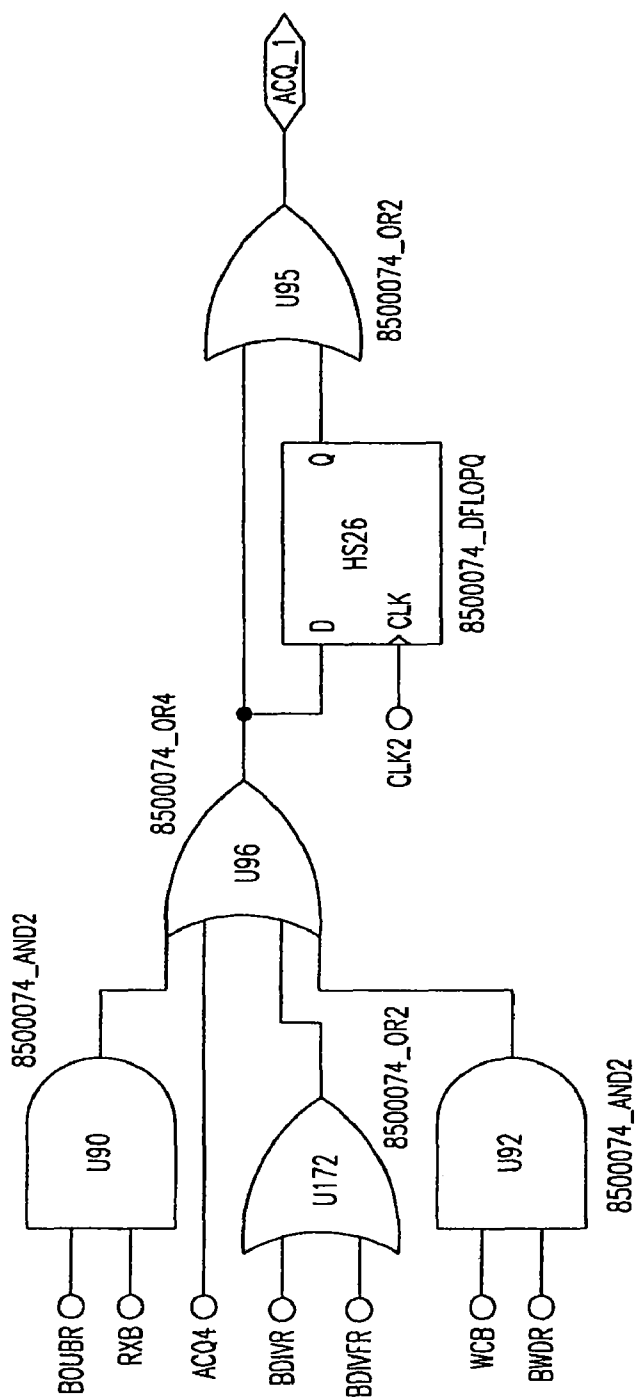
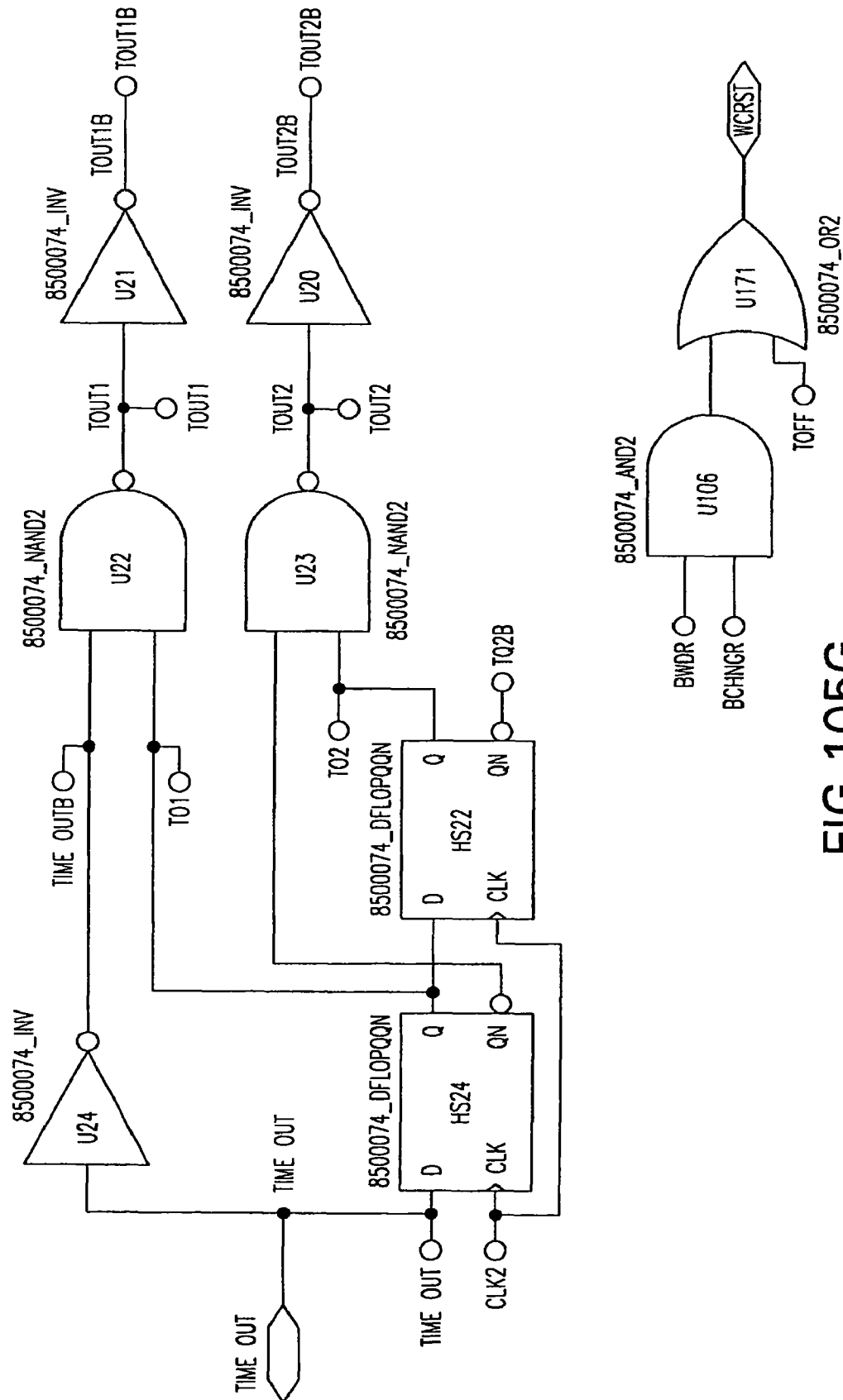


FIG. 105F



**FIG. 105G**

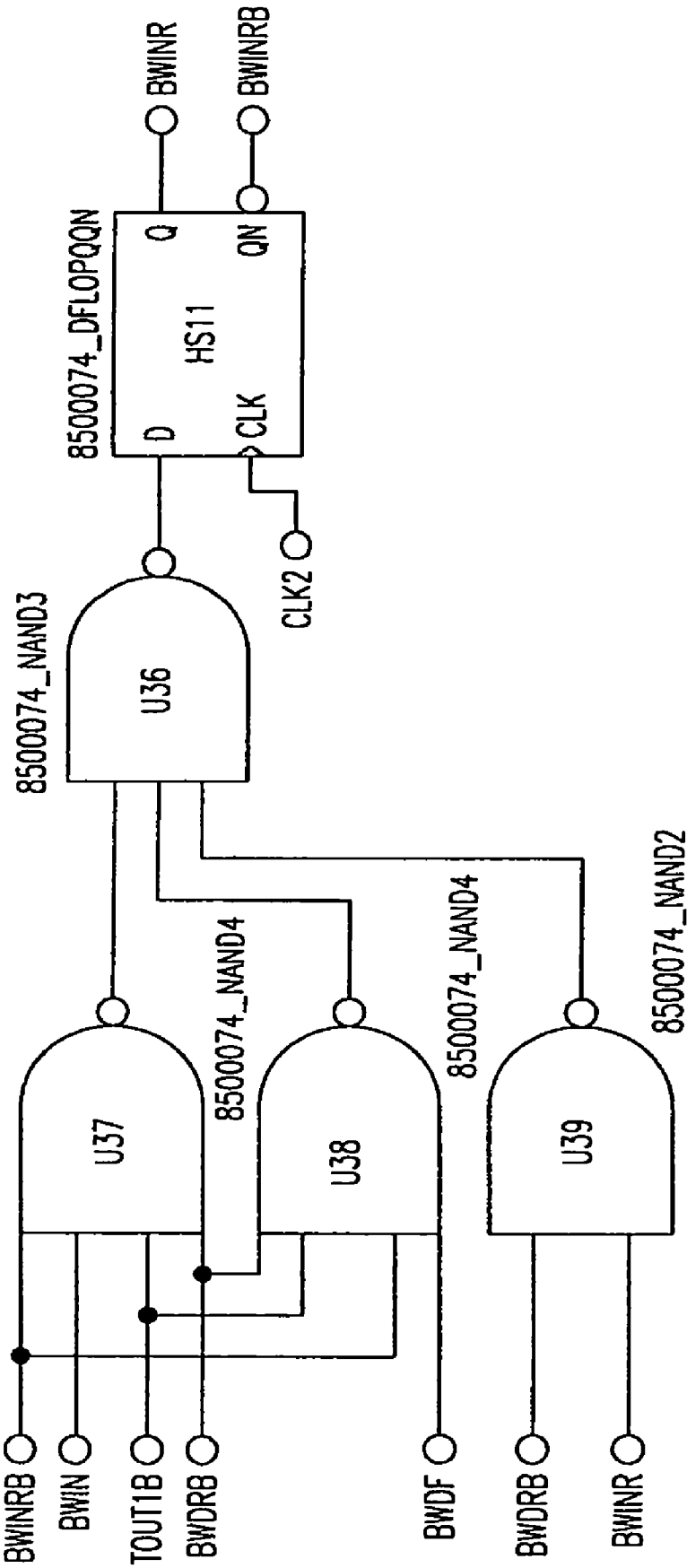


FIG.105H

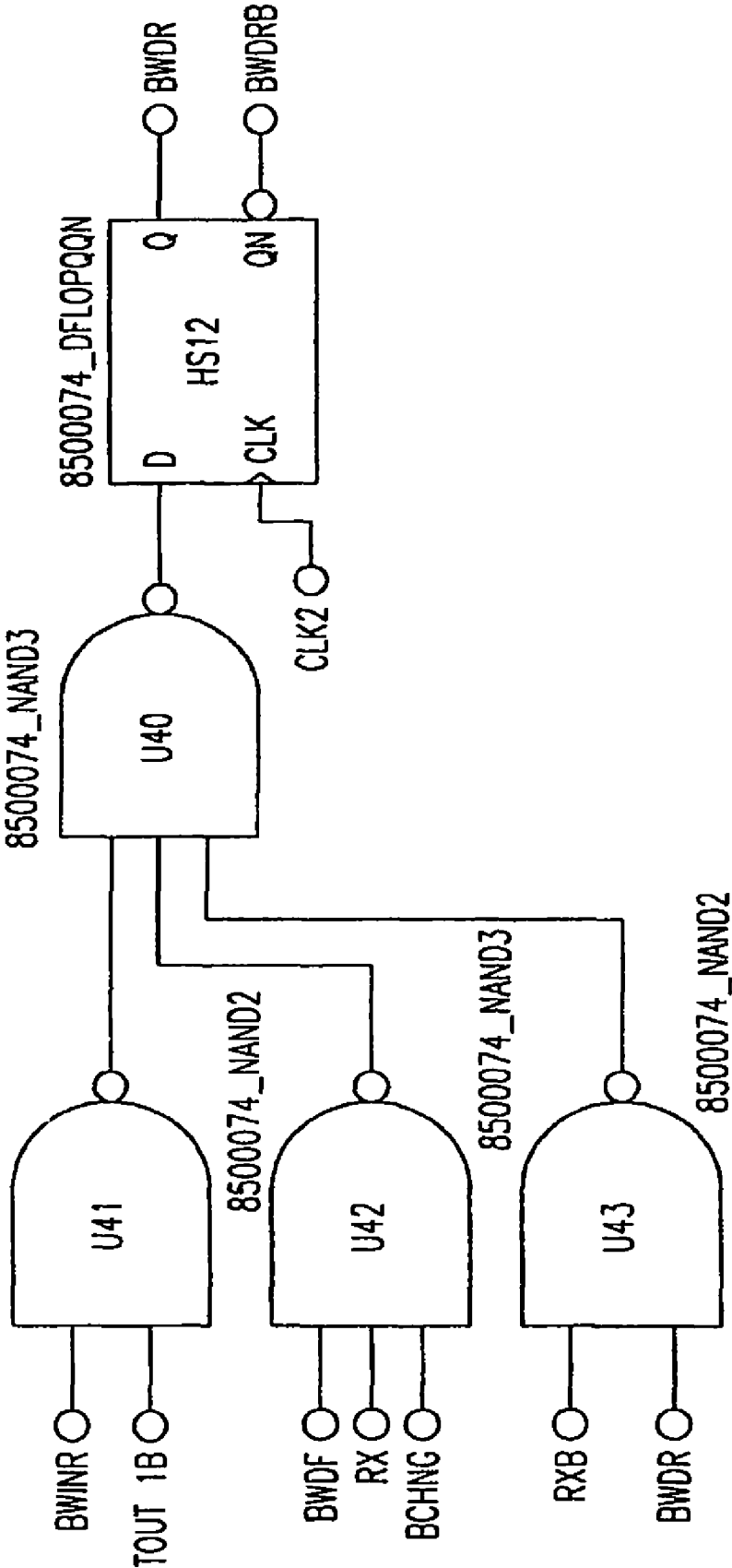


FIG. 105I



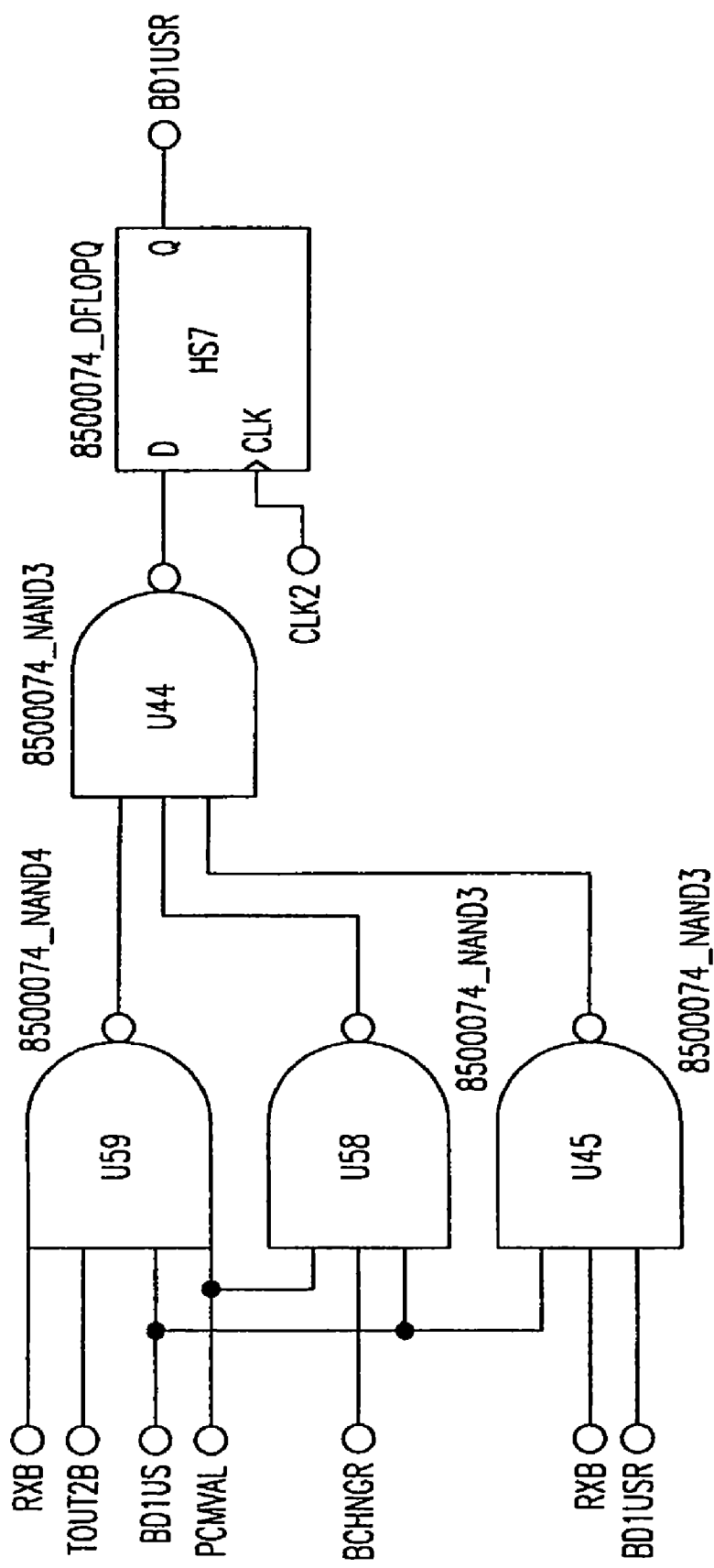


FIG. 105J

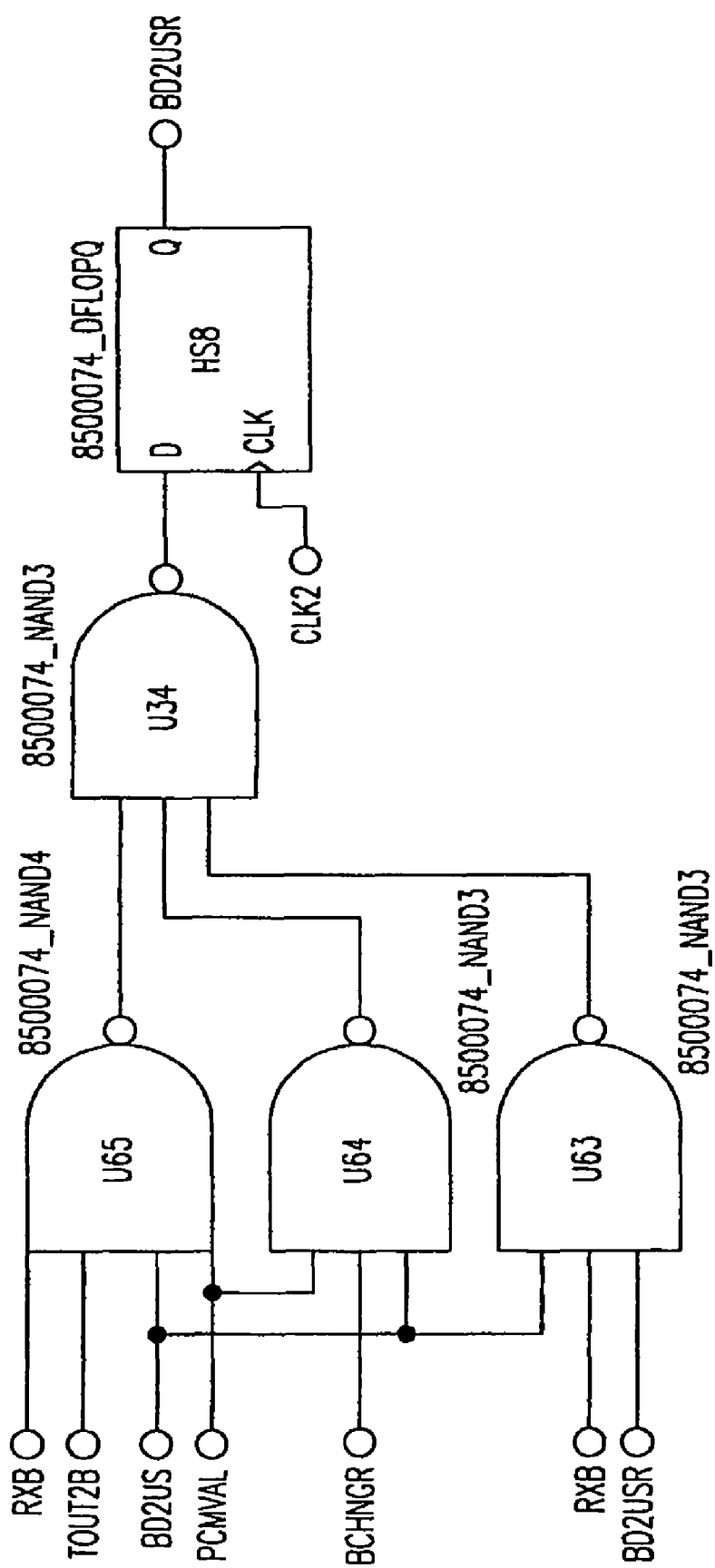


FIG. 105K

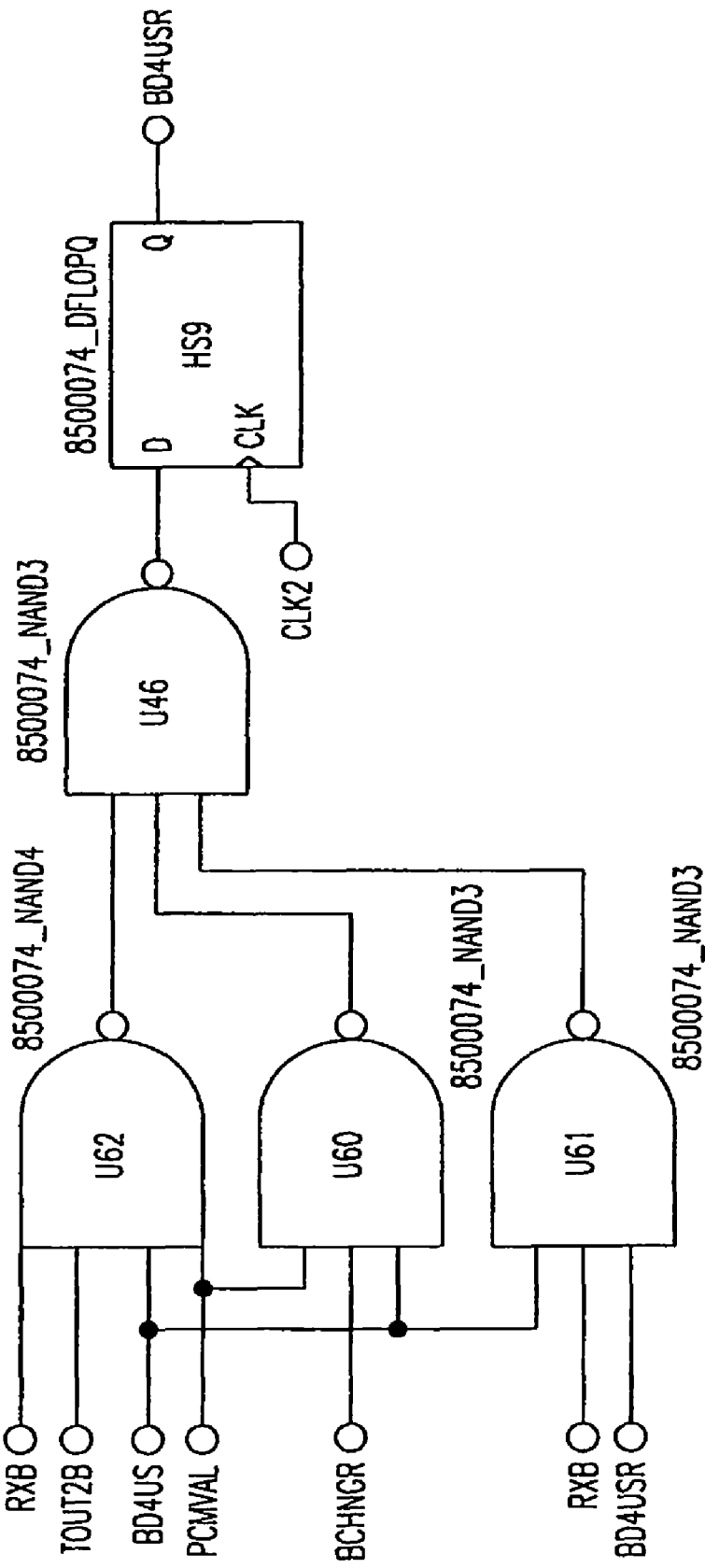


FIG. 105L

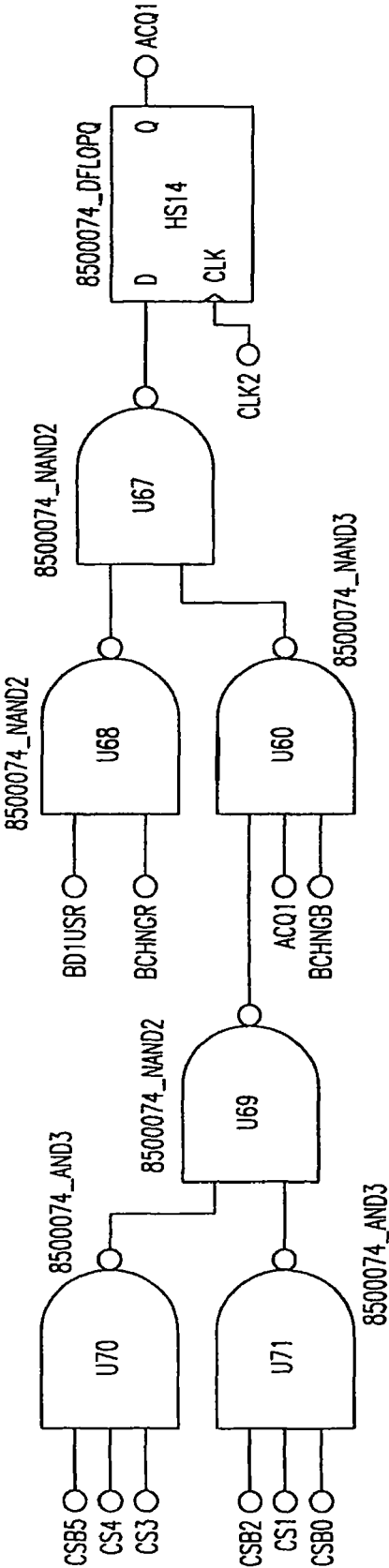


FIG. 105M

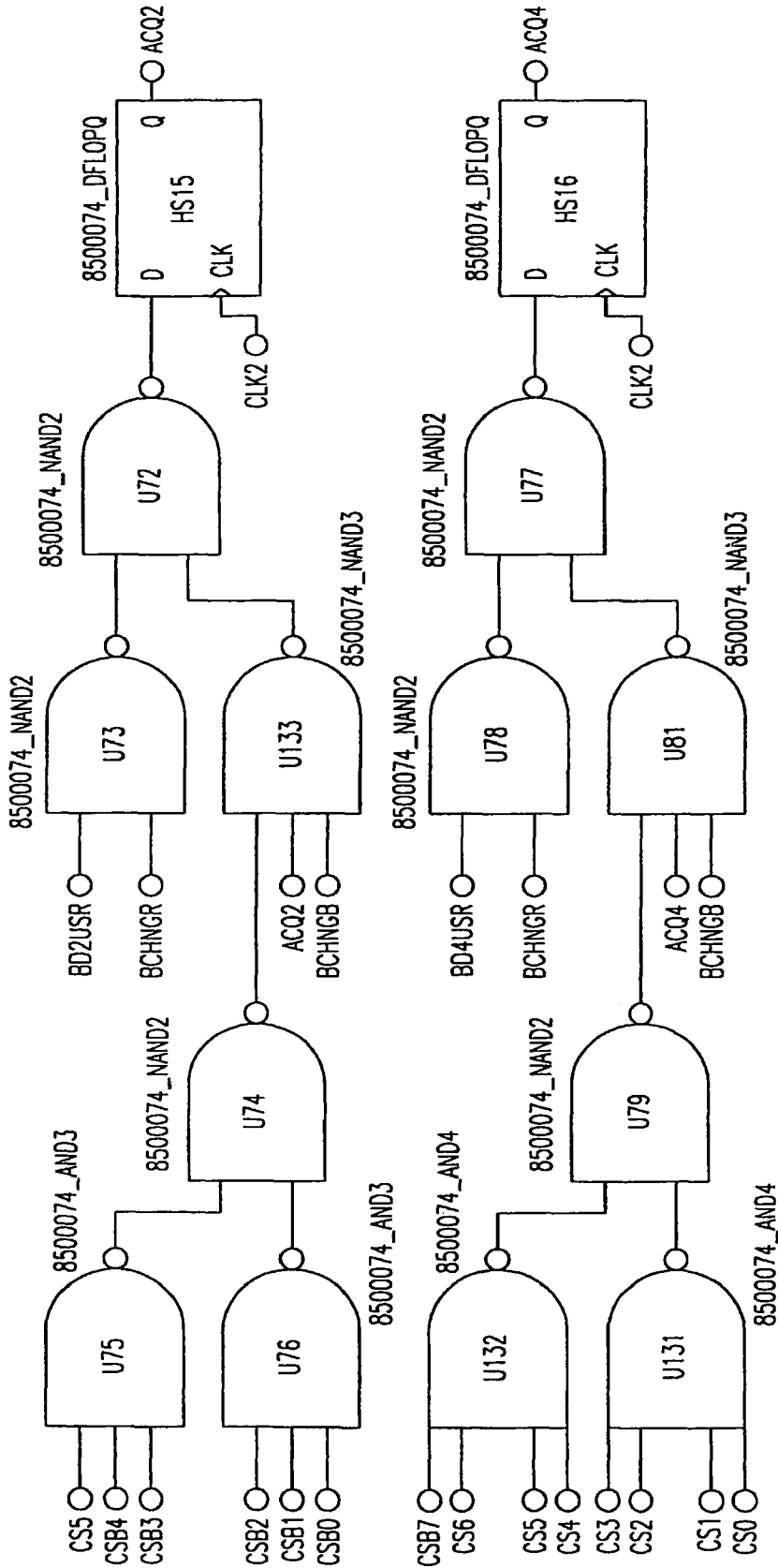


FIG. 105N

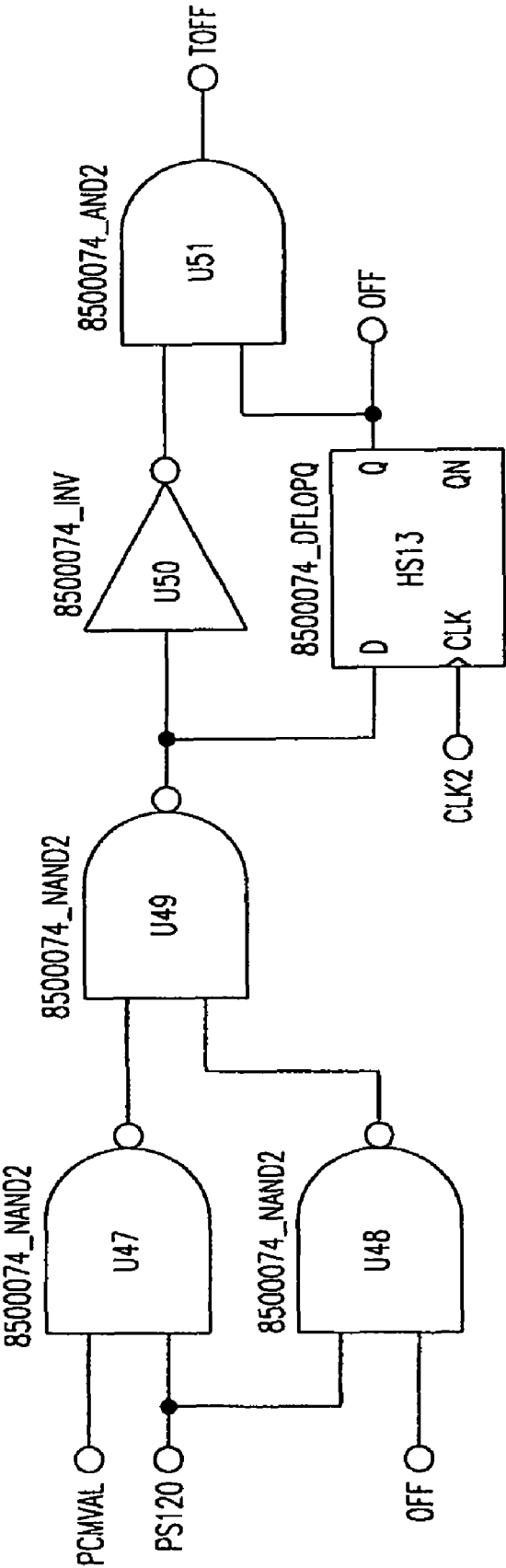


FIG. 1050

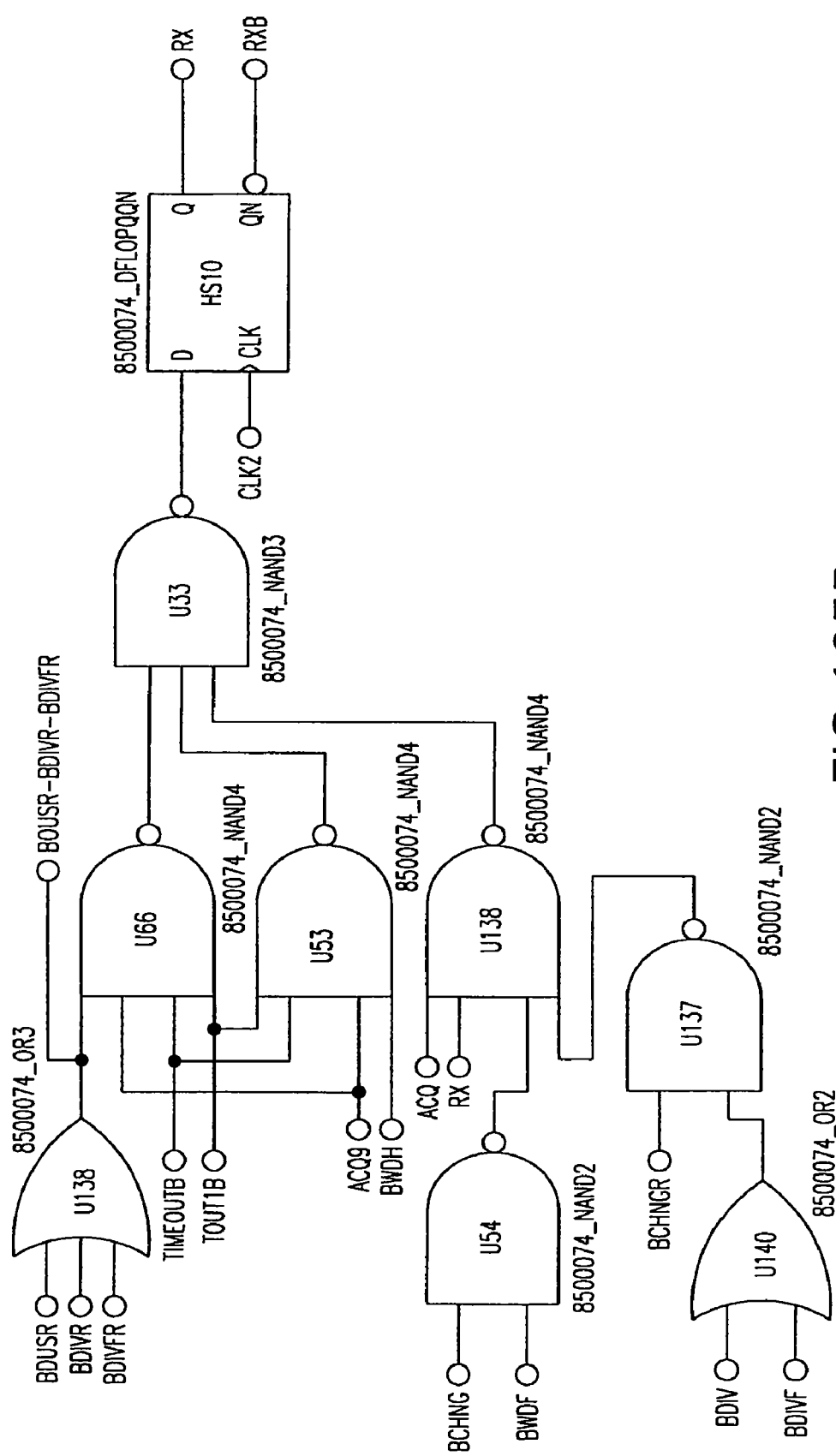
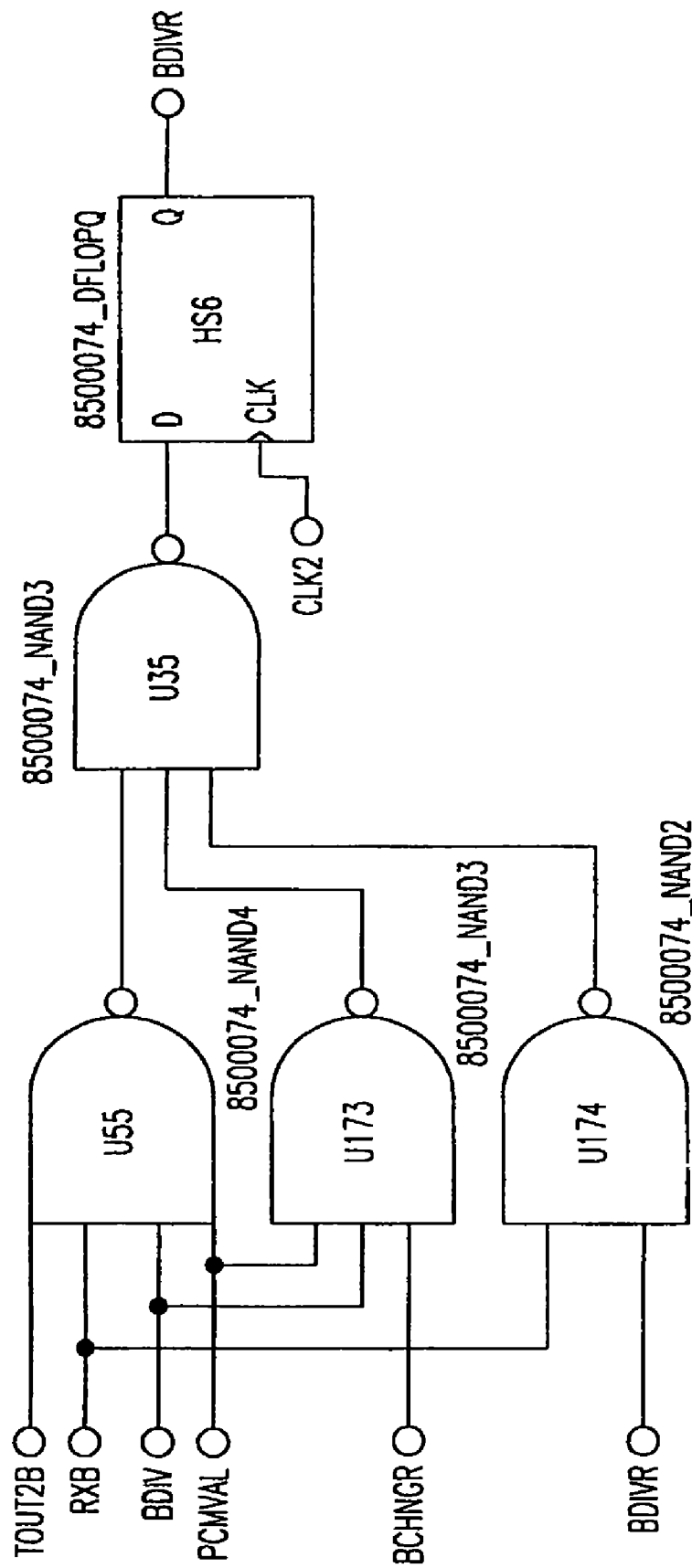


FIG.105P



**FIG. 105Q**



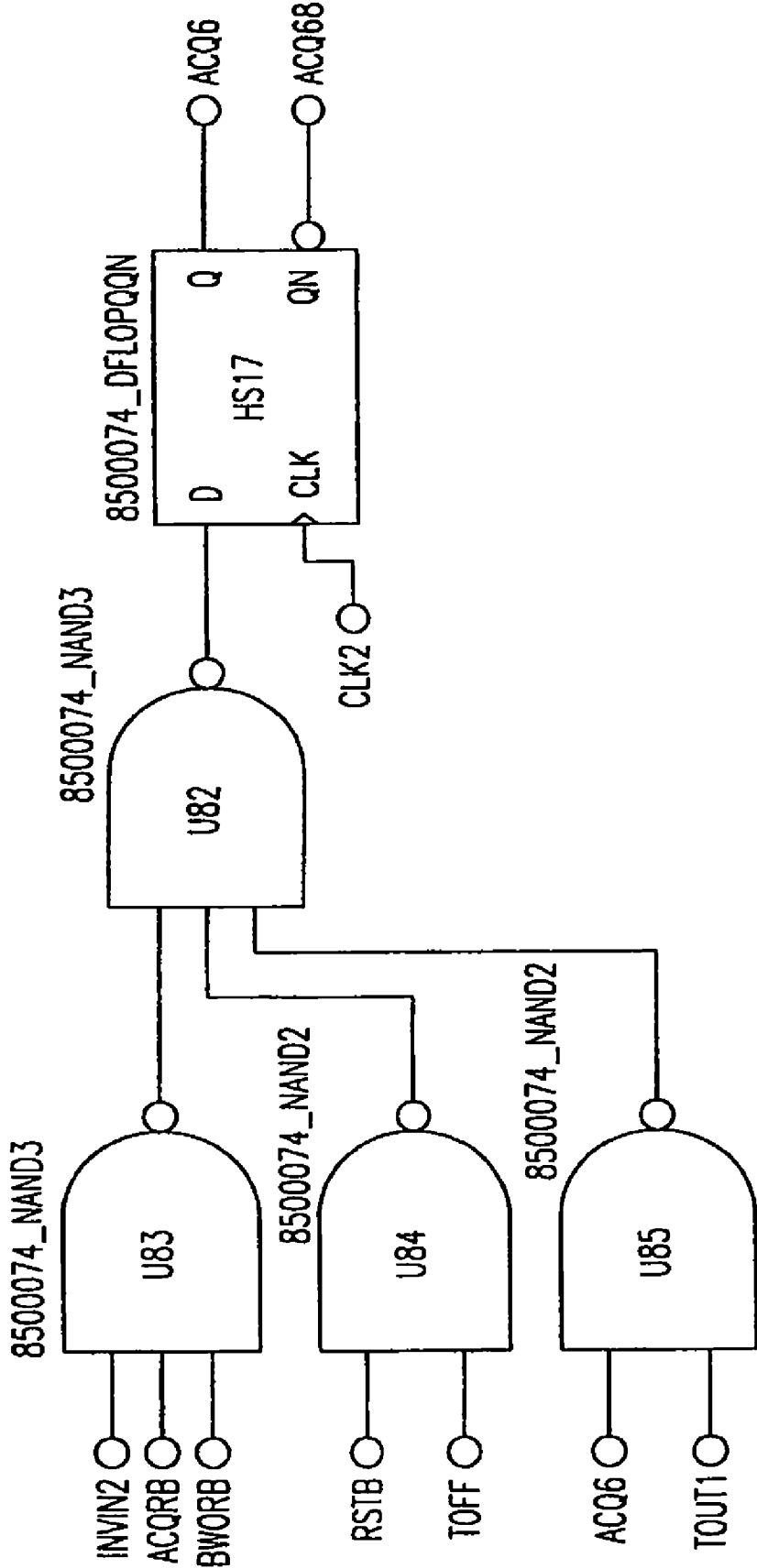


FIG. 105R

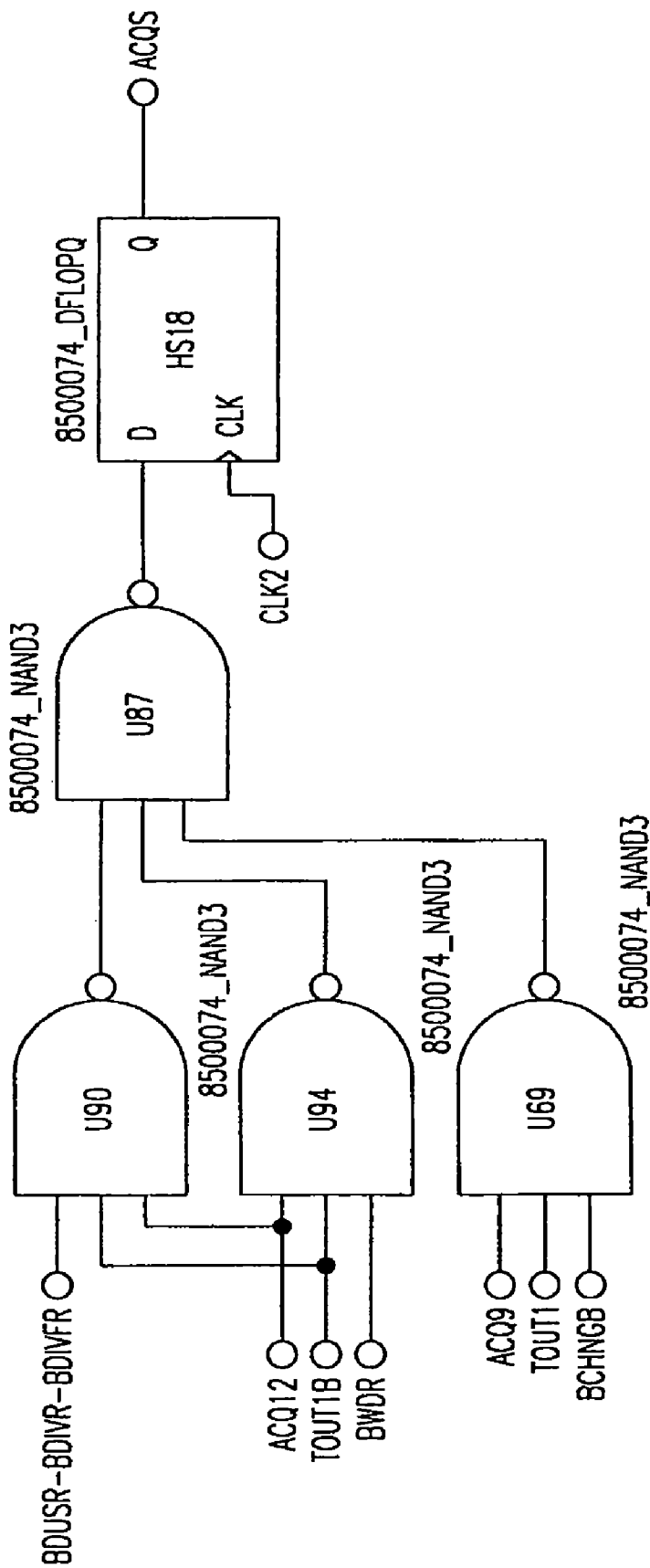


FIG. 105S

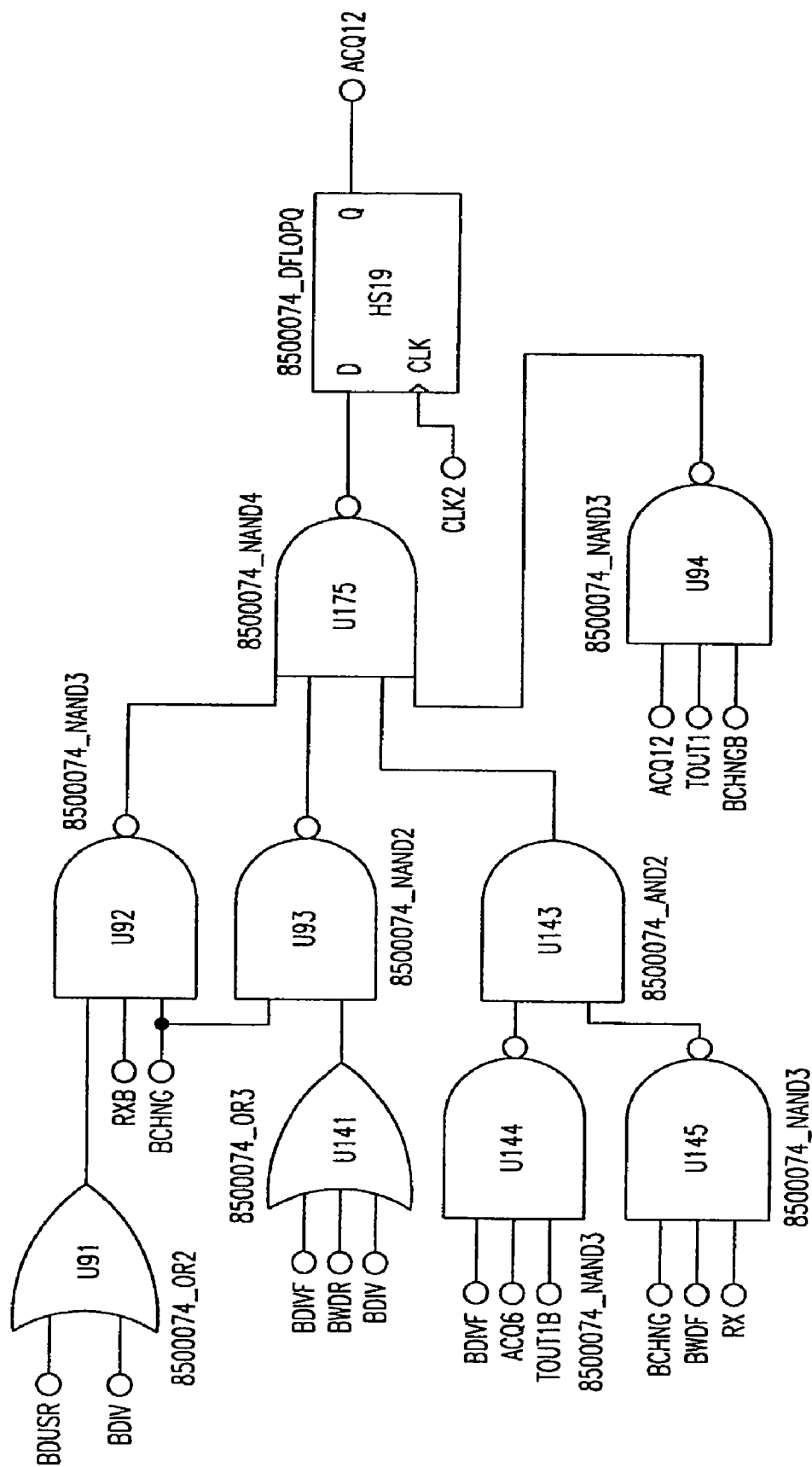


FIG. 105T

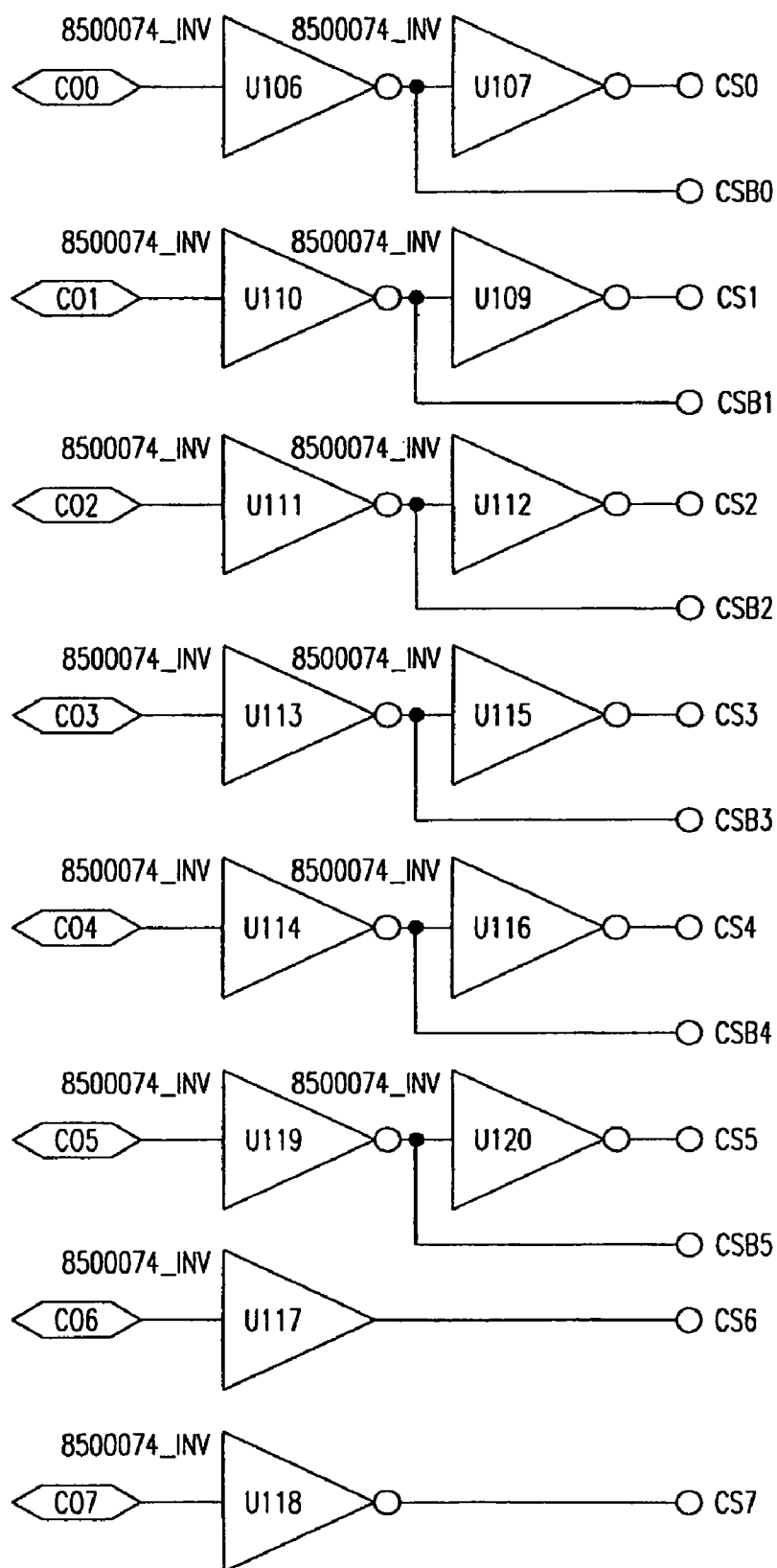


FIG. 105U

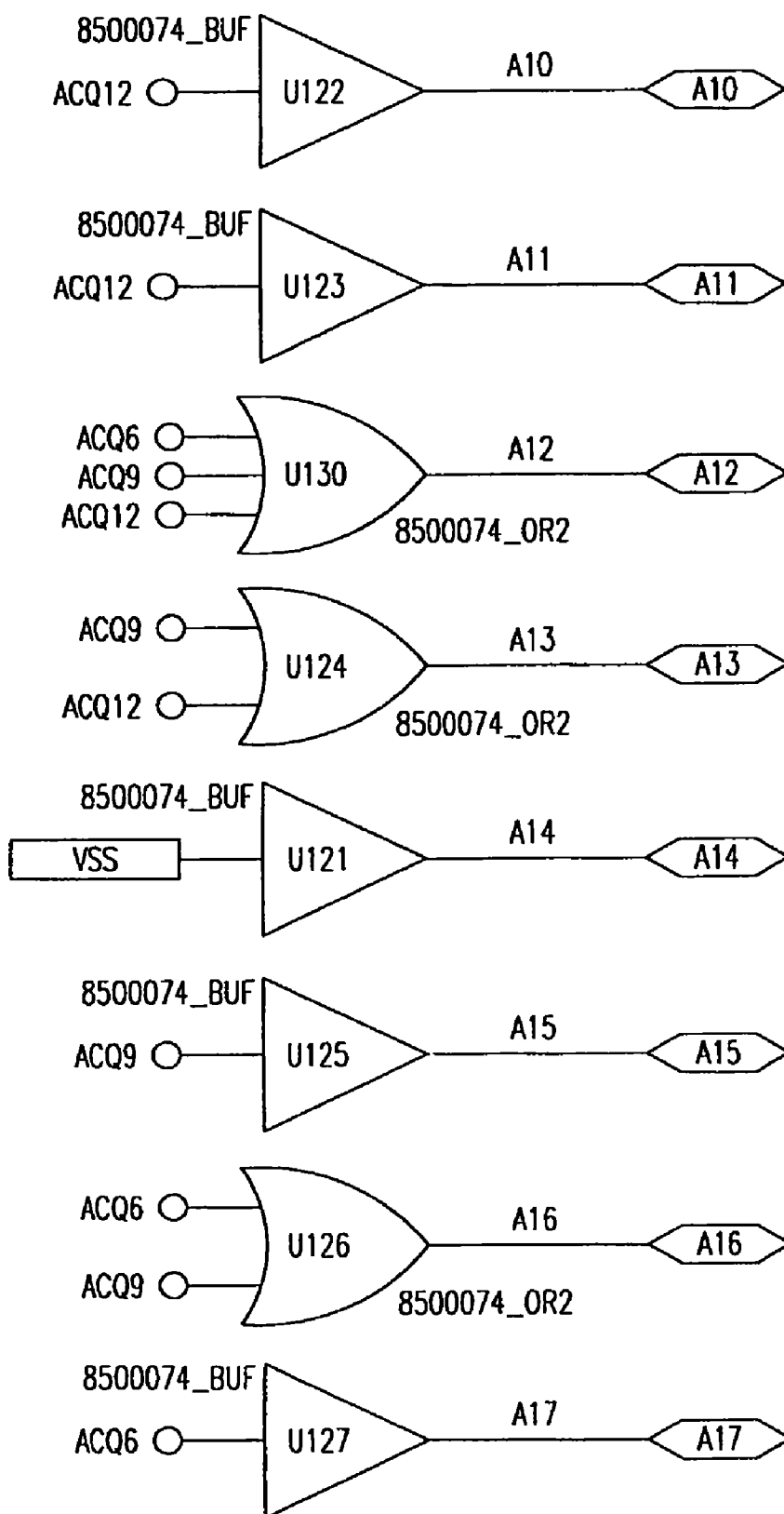


FIG. 105V

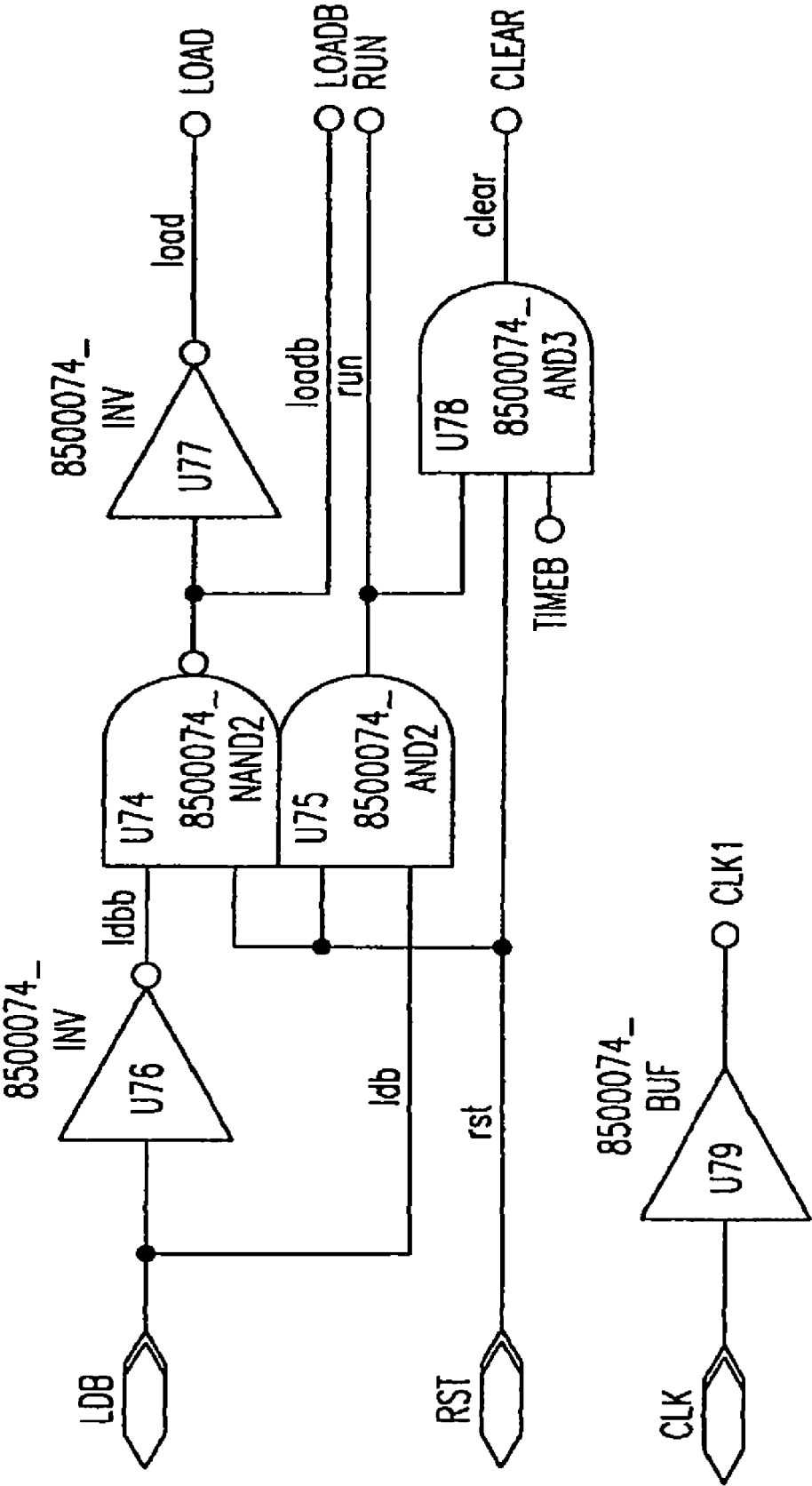


FIG. 106A

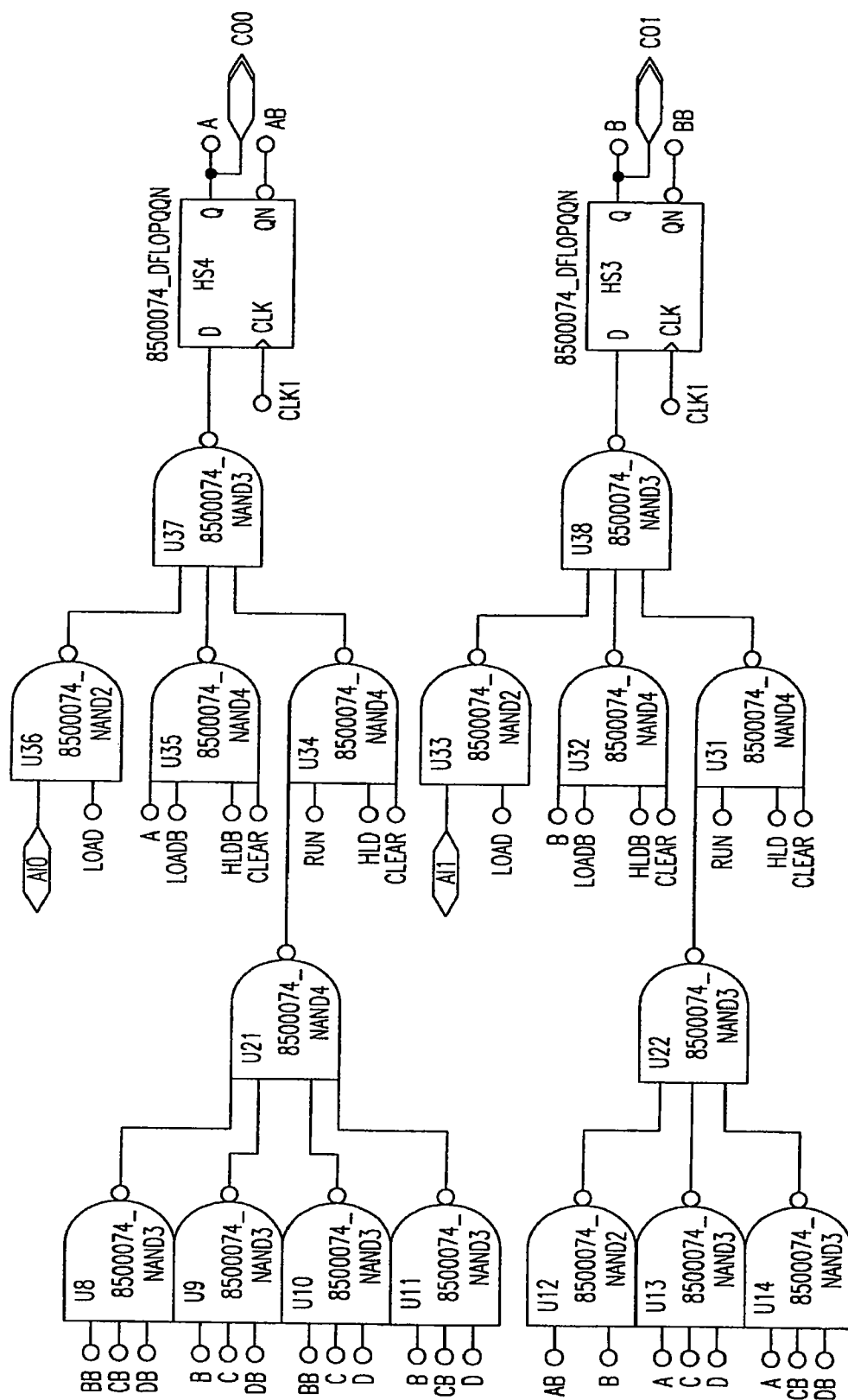


FIG. 106B

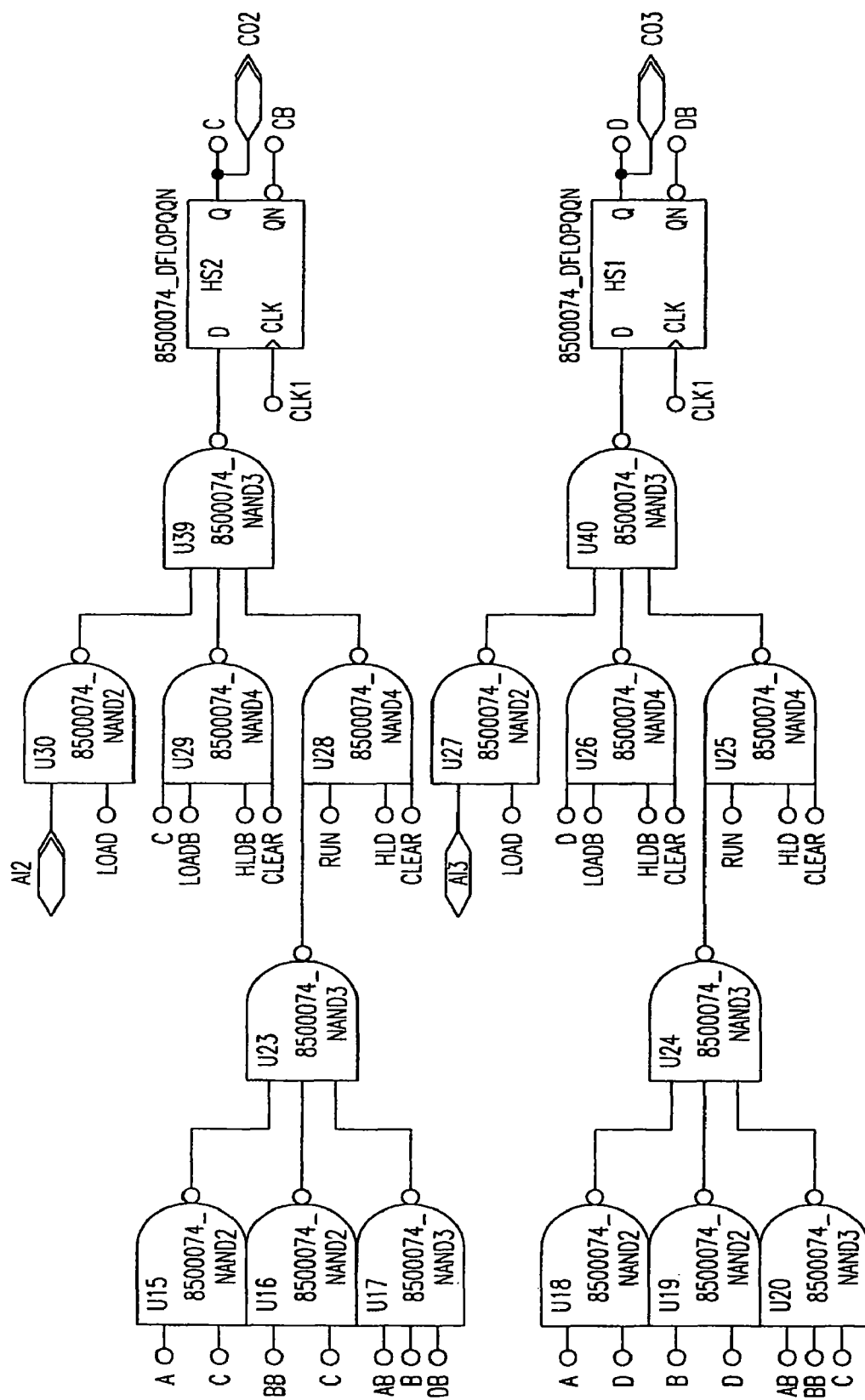


FIG. 106C



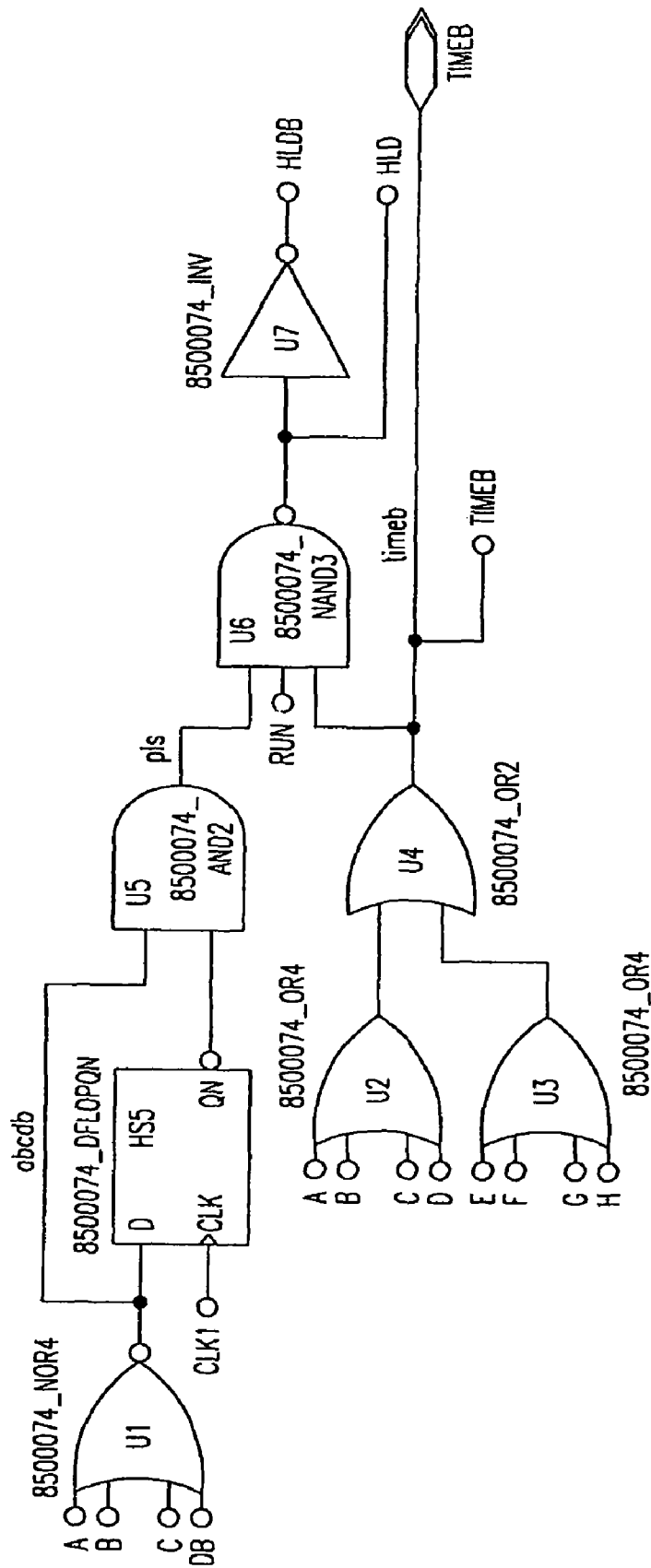


FIG. 106D

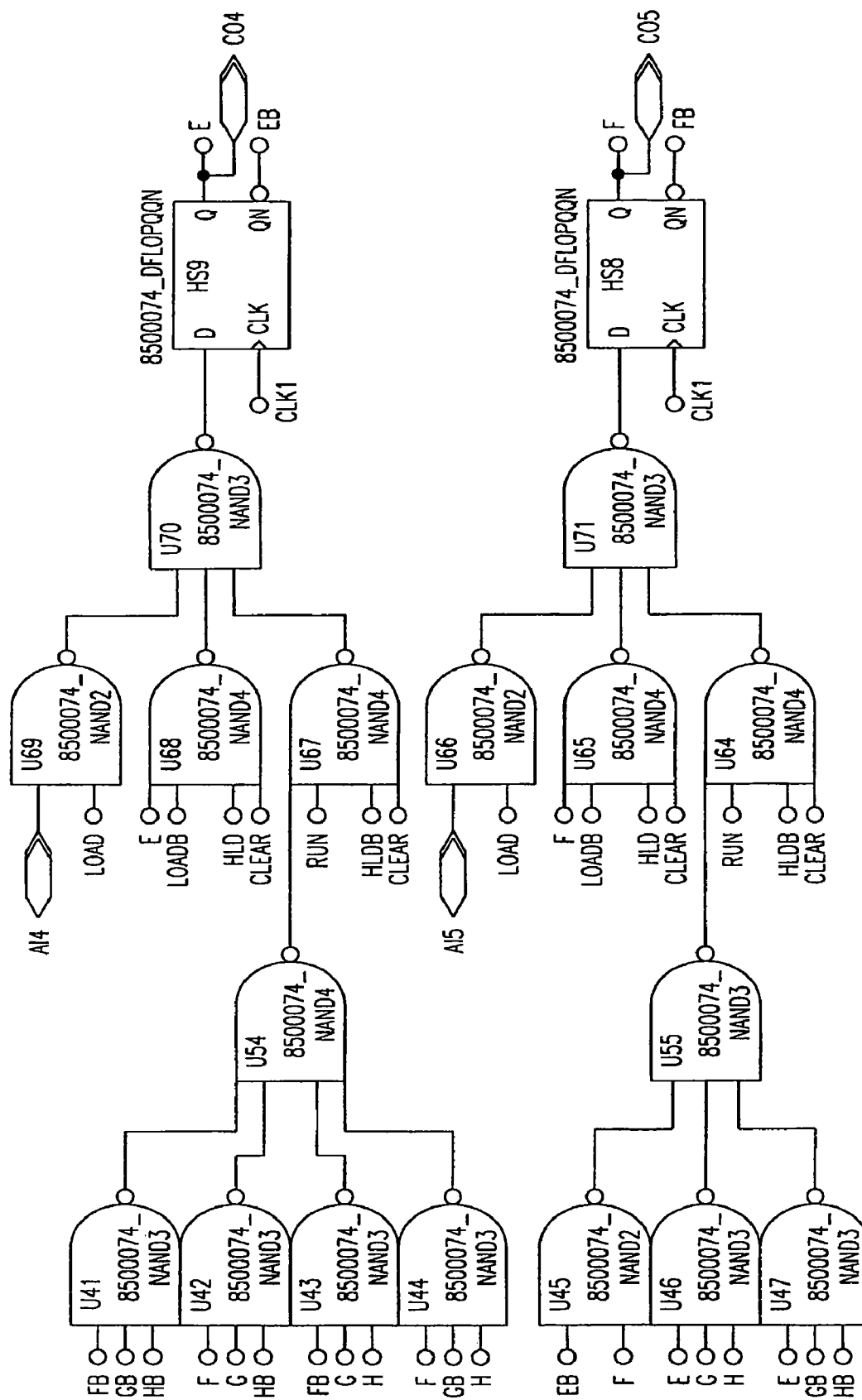


FIG. 106E

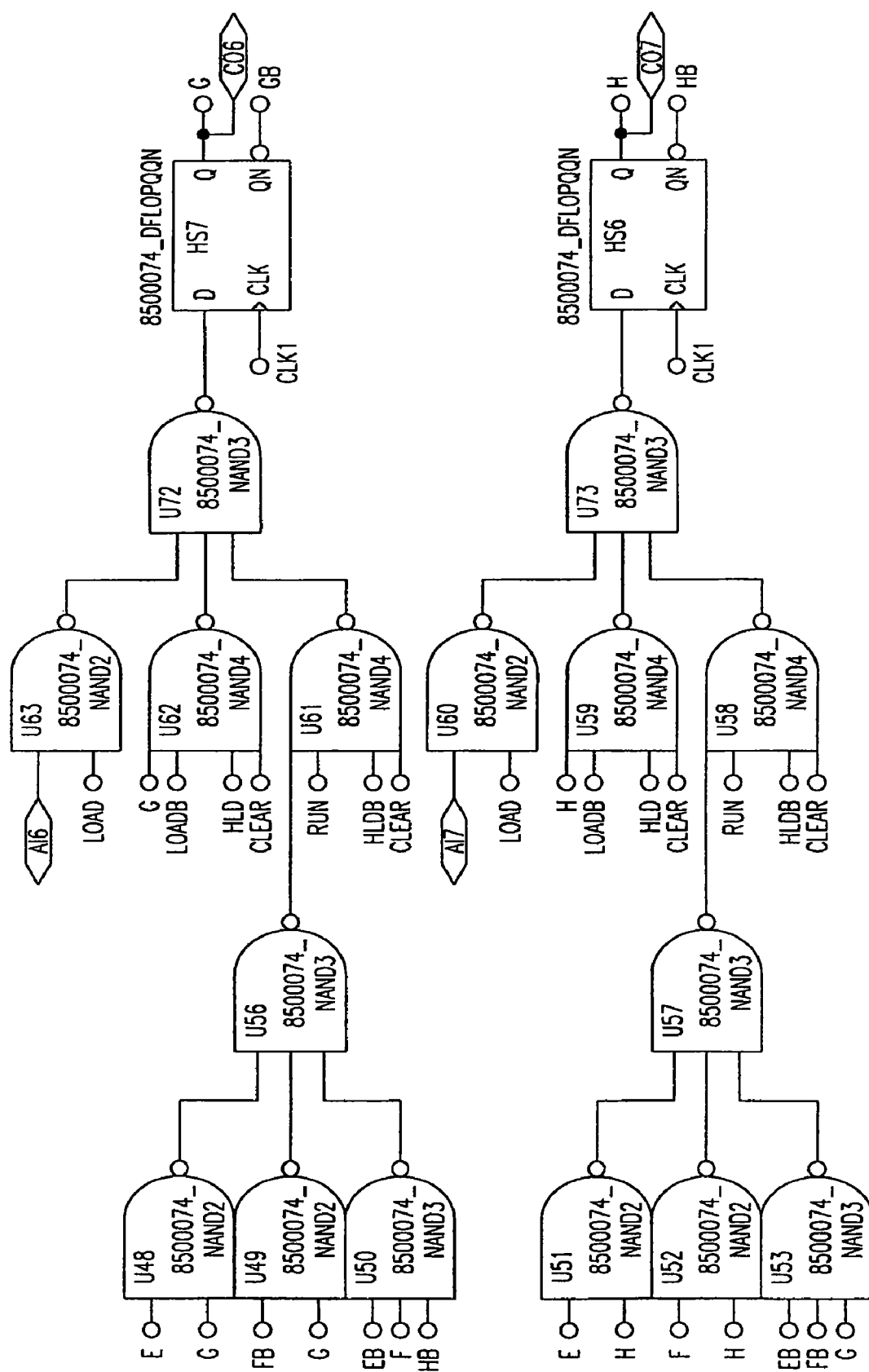
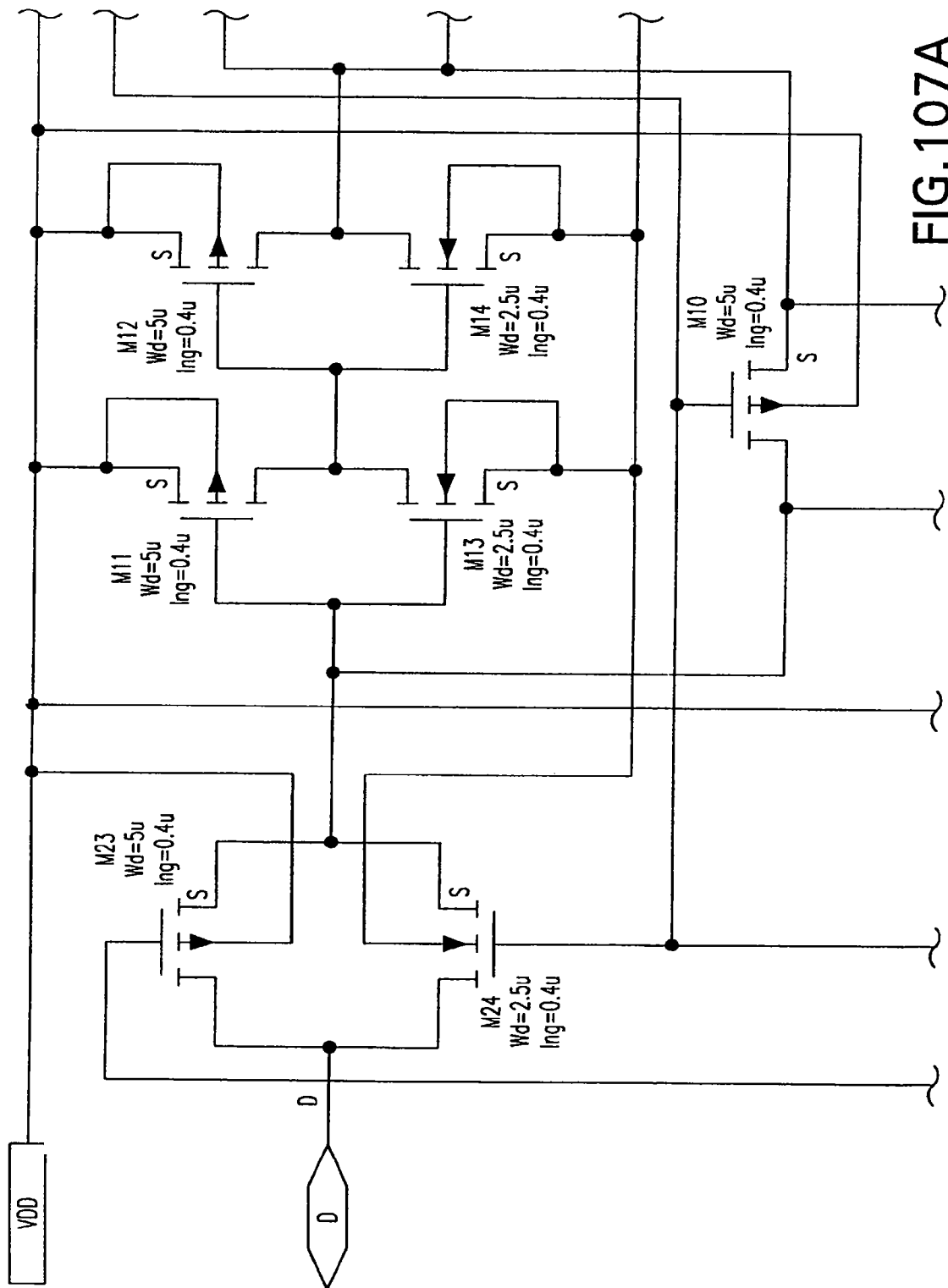


FIG. 106F



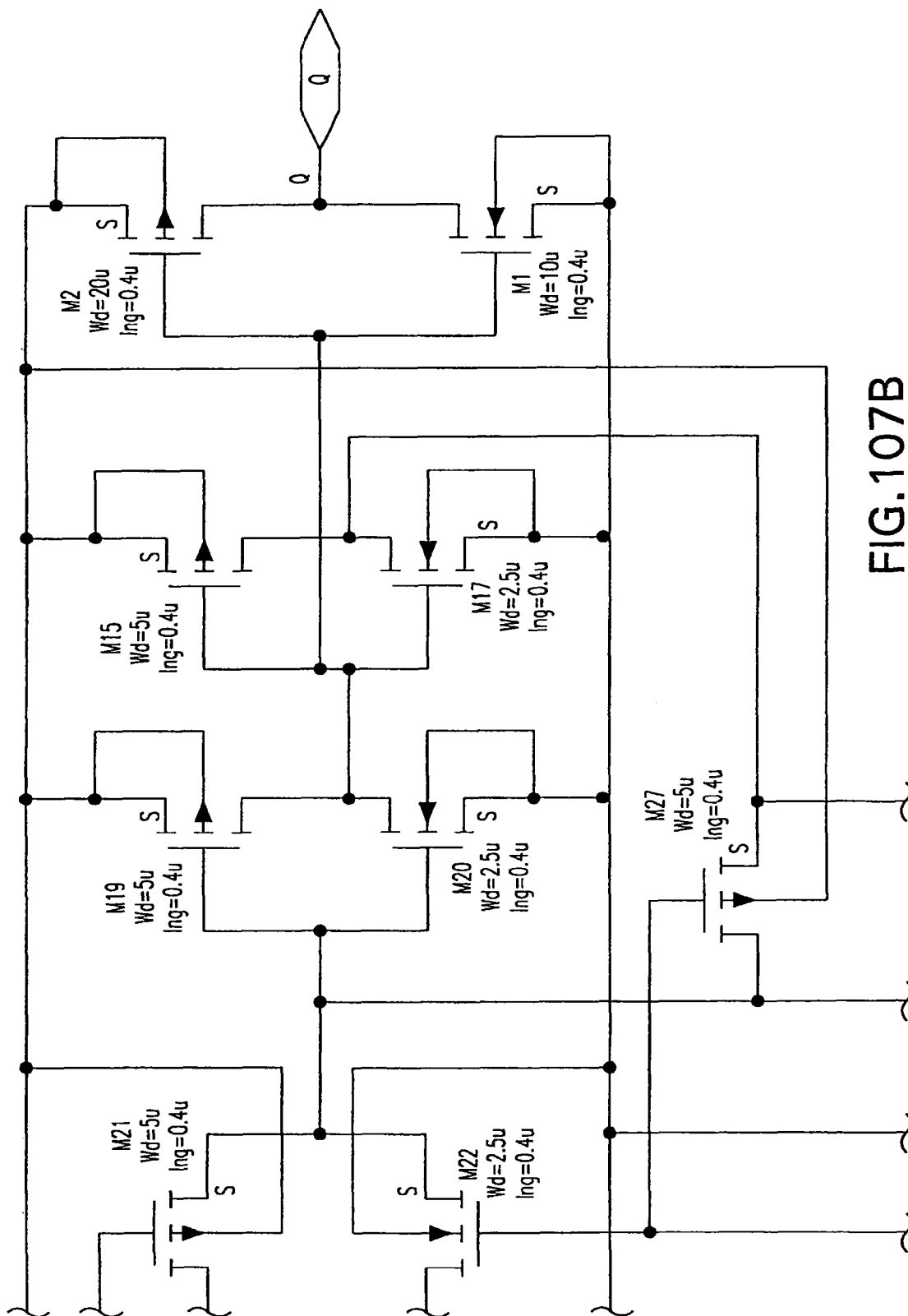
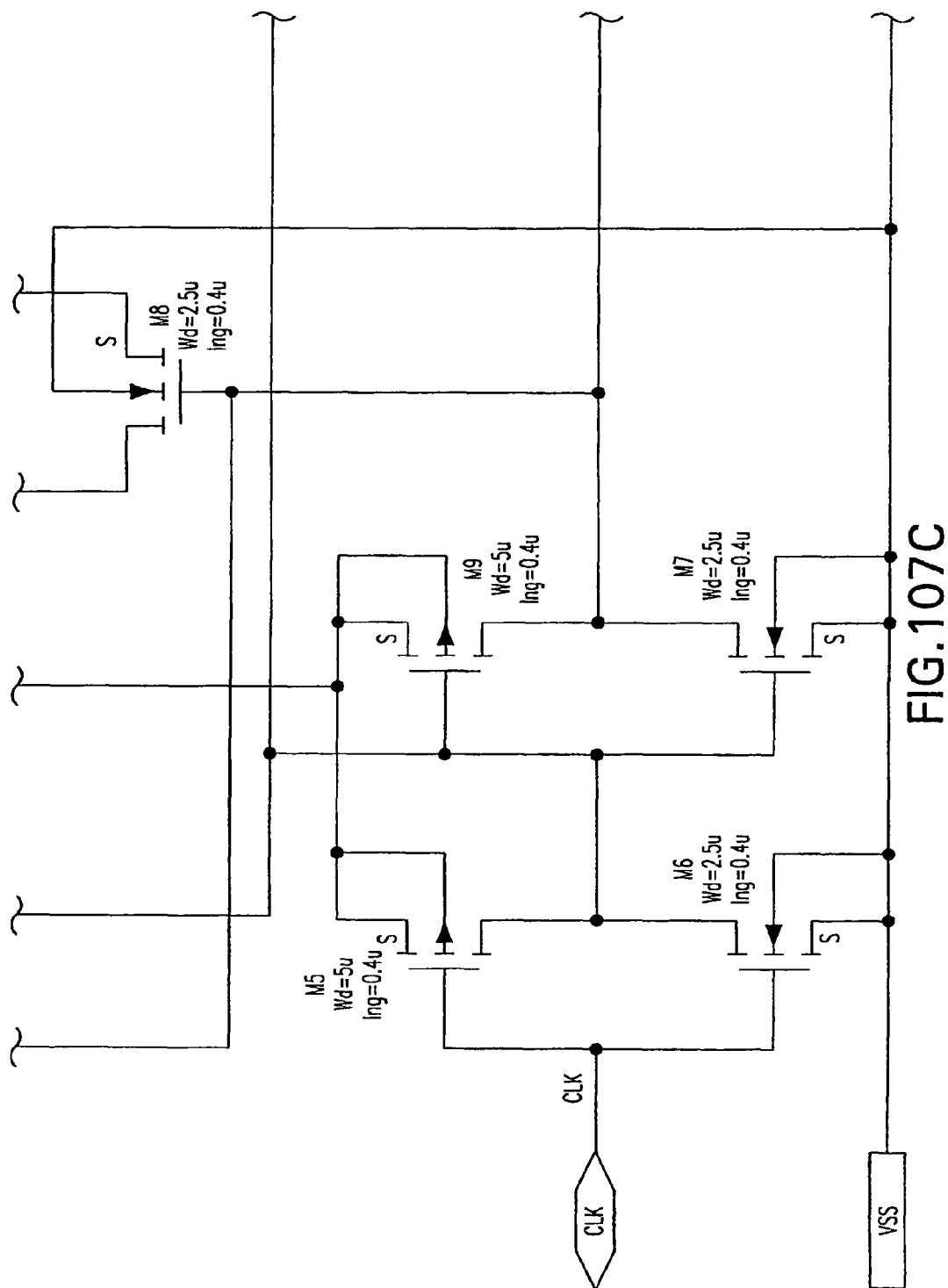


FIG.107B



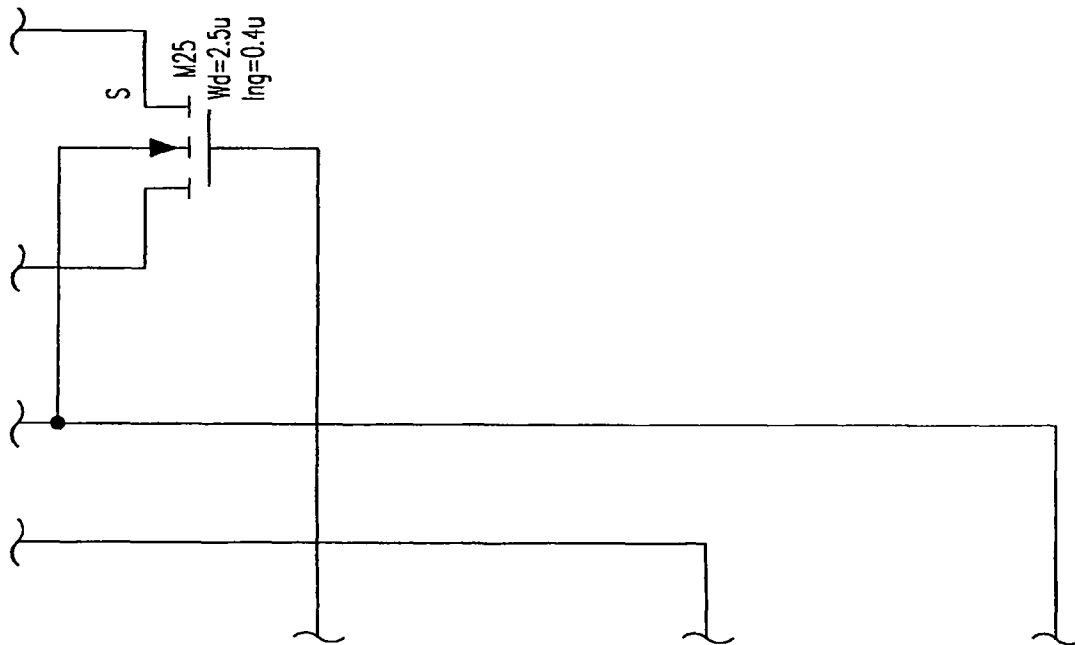


FIG. 107D

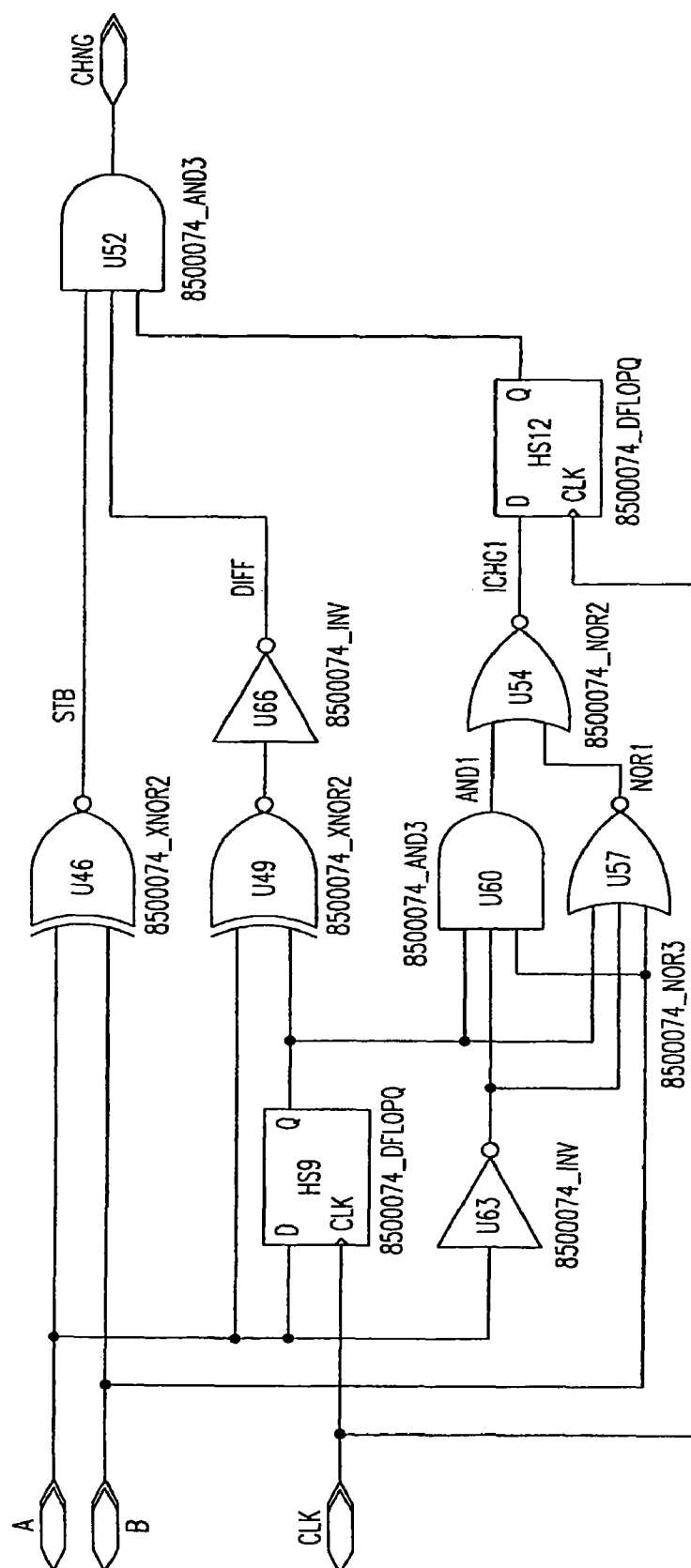


FIG. 108



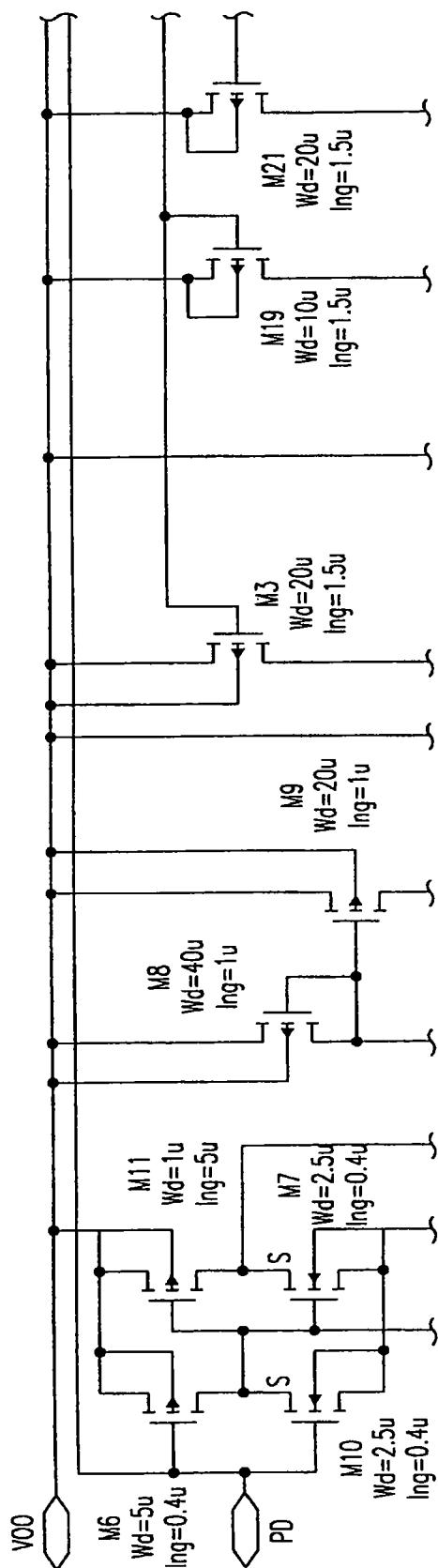


FIG. 109A

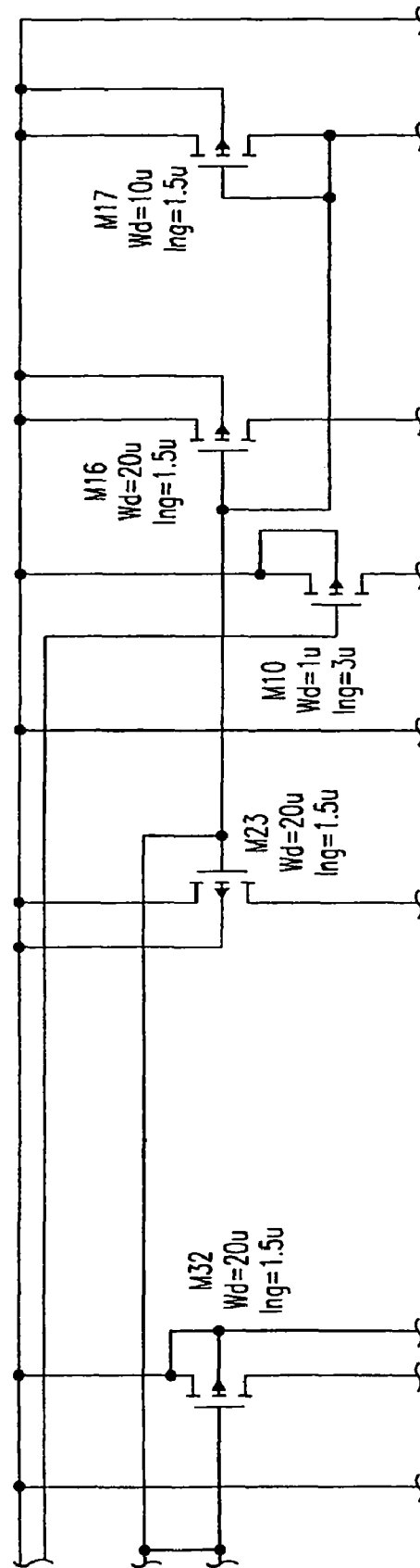


FIG. 109B

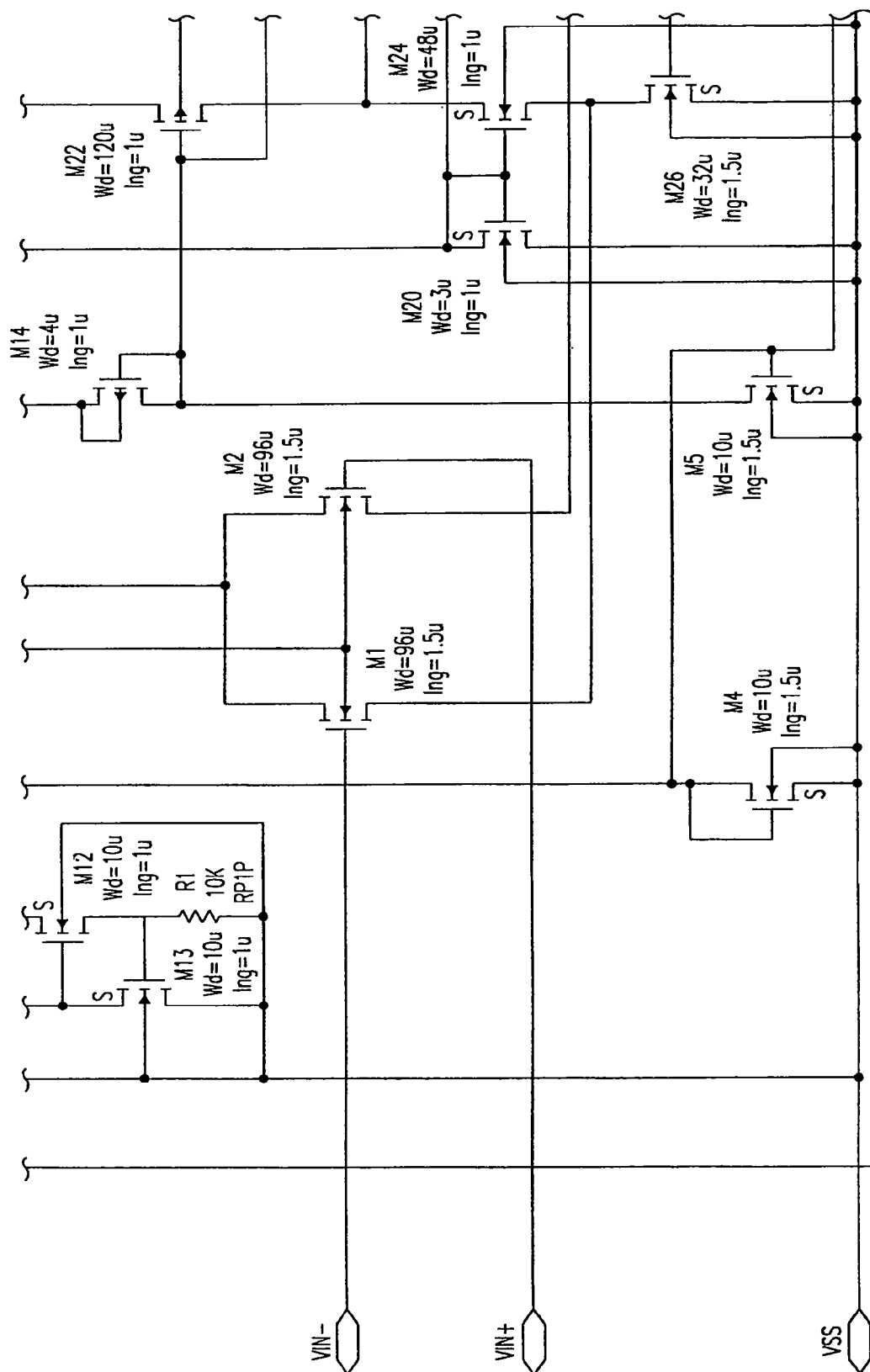


FIG. 109C

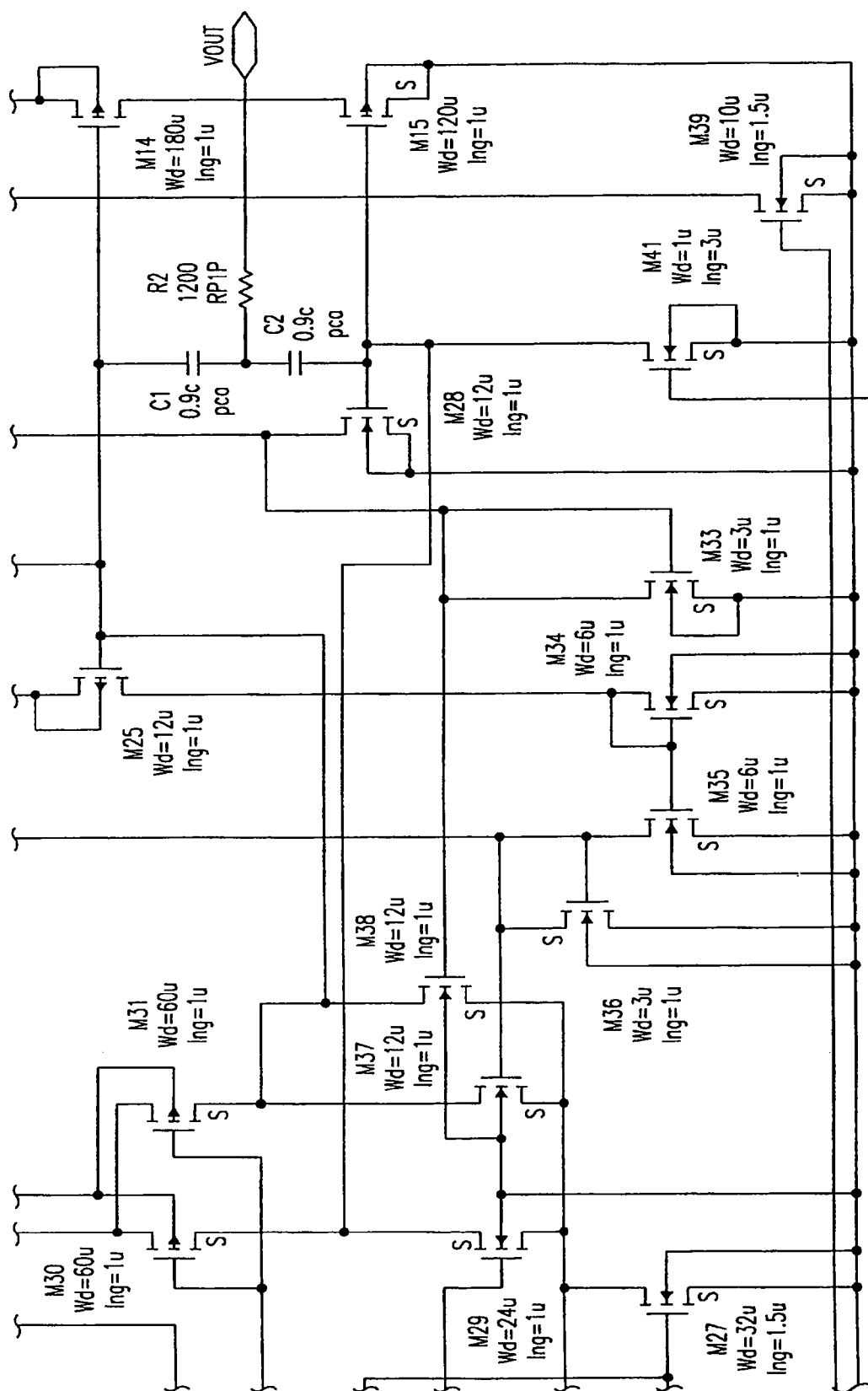


FIG. 109D

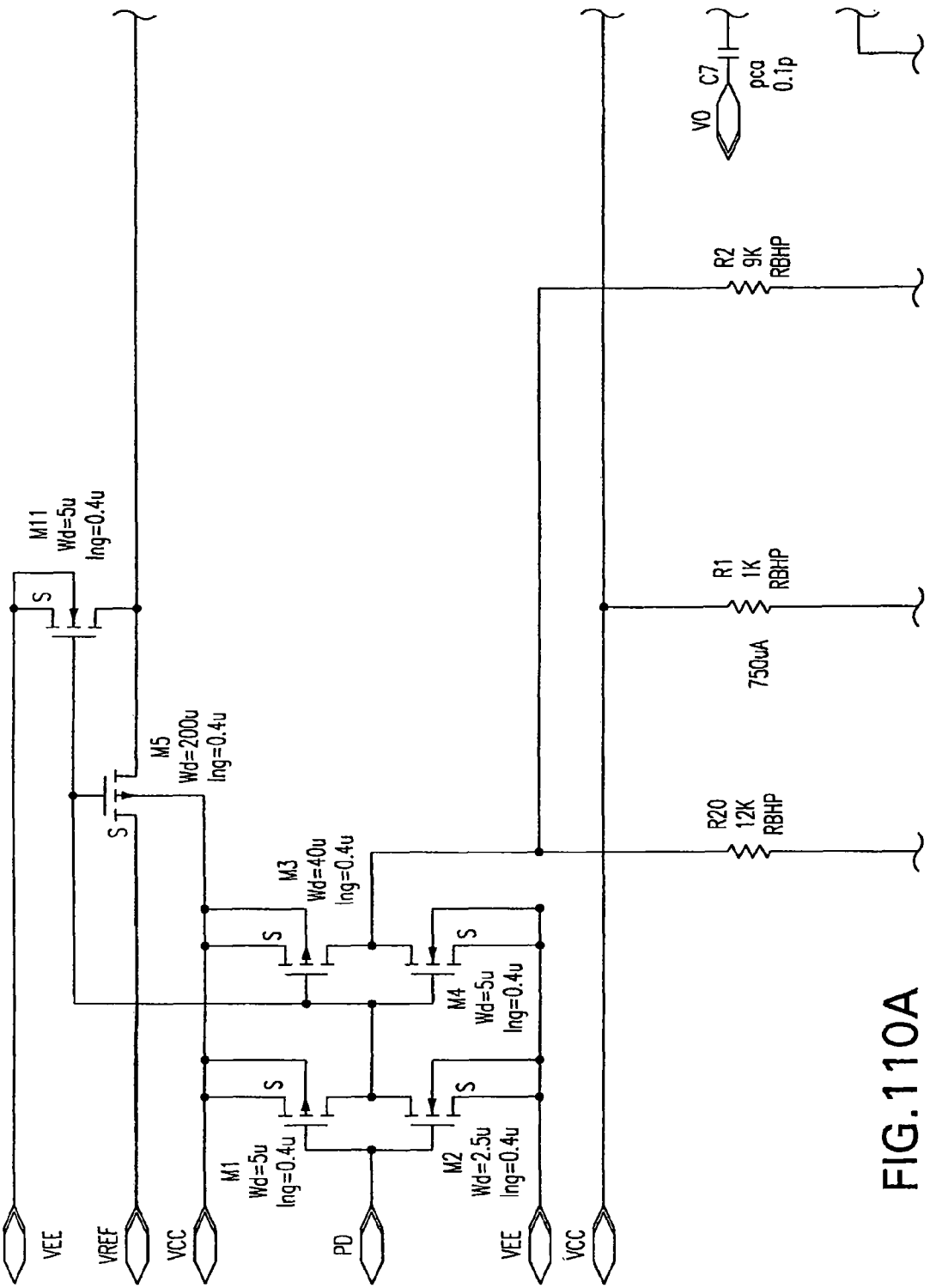
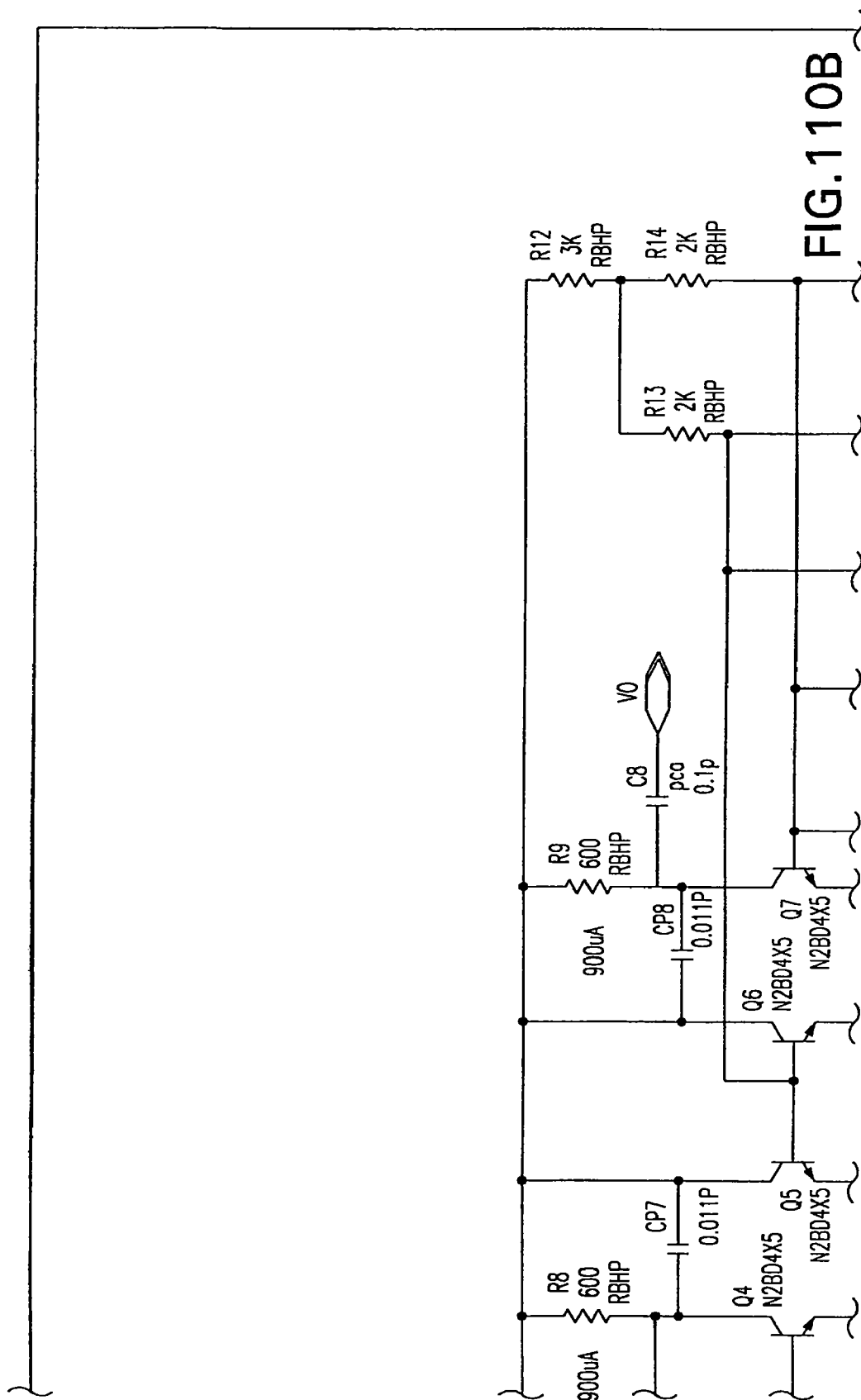


FIG.110A



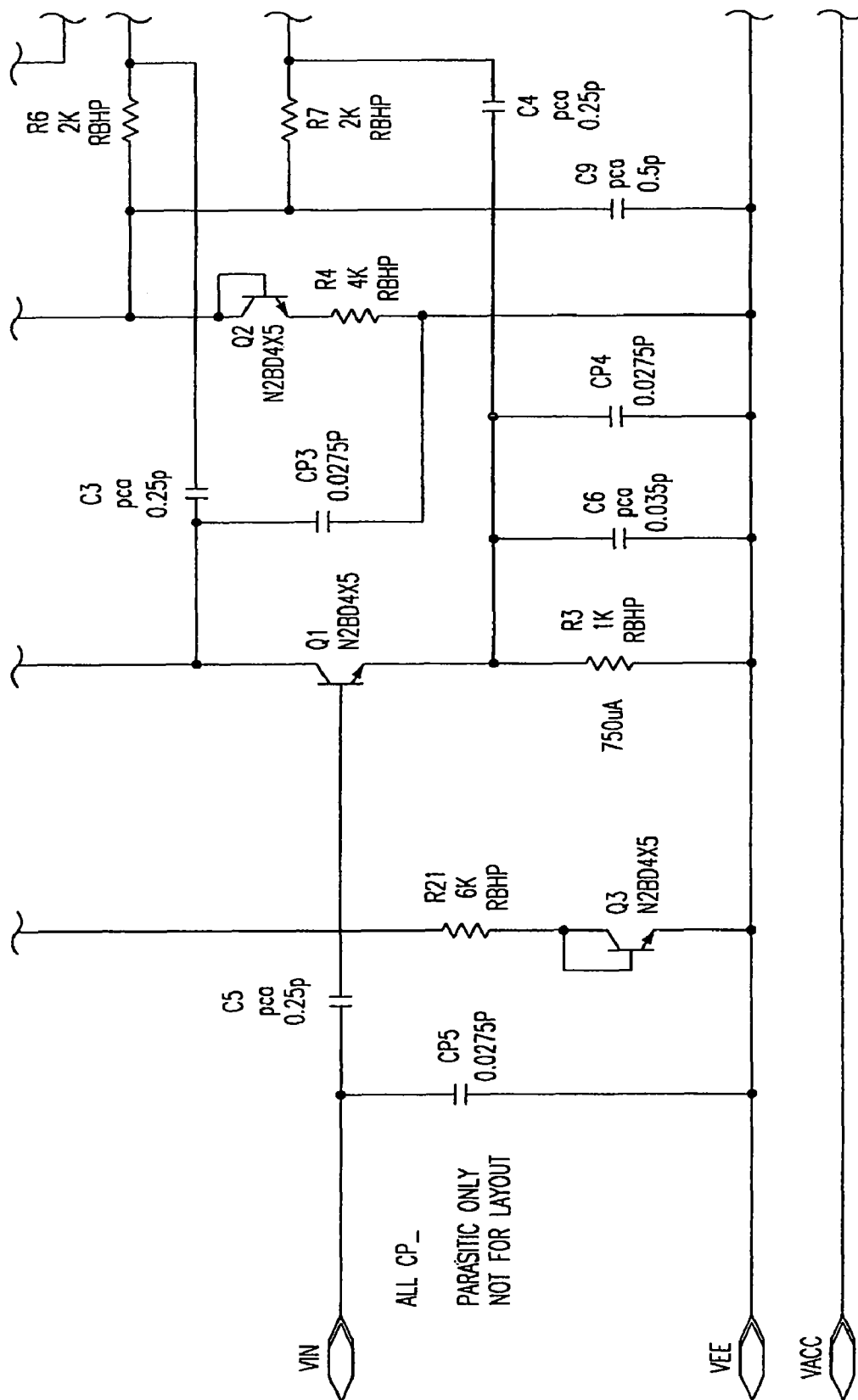


FIG. 110C

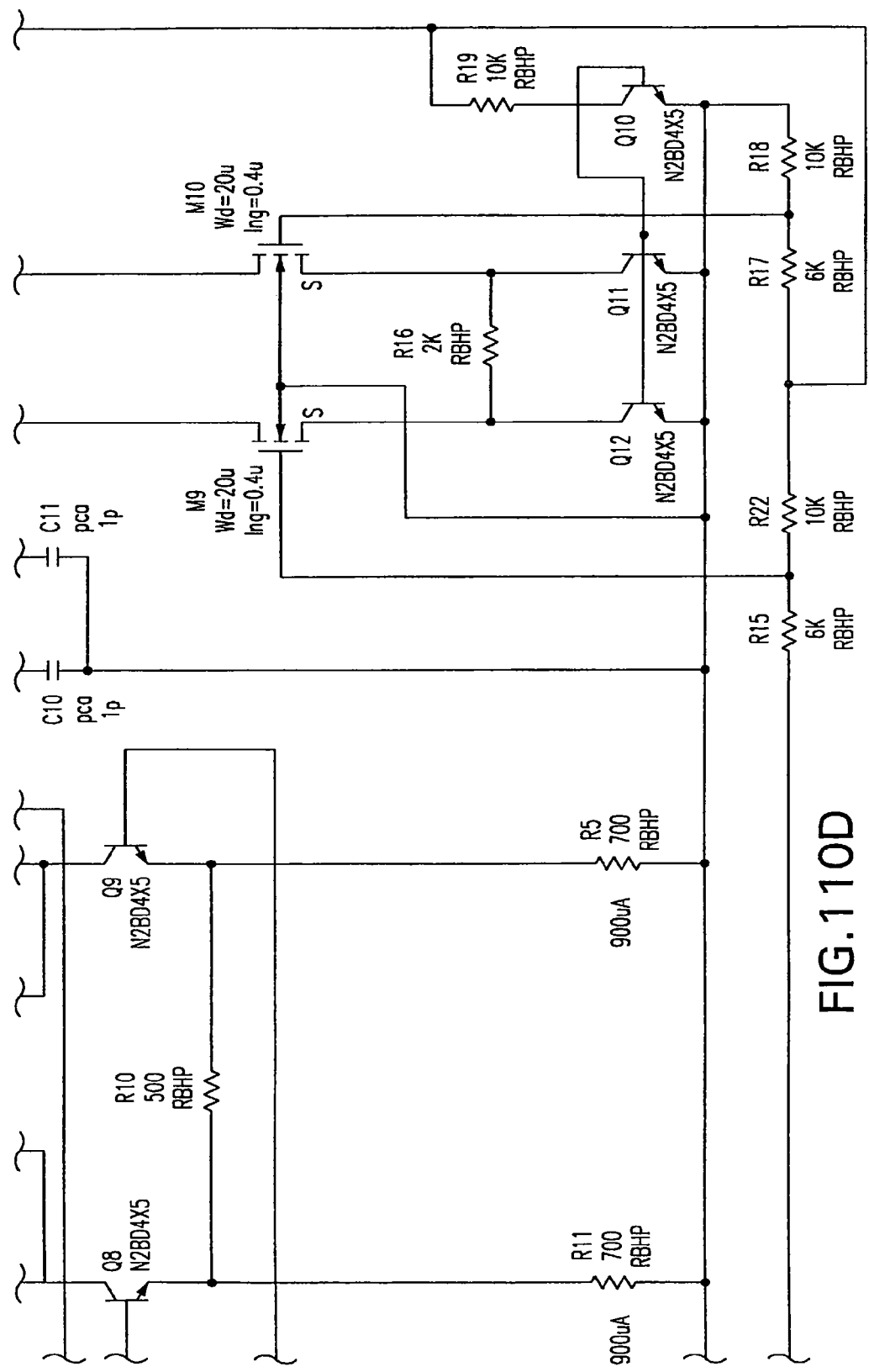


FIG. 110D



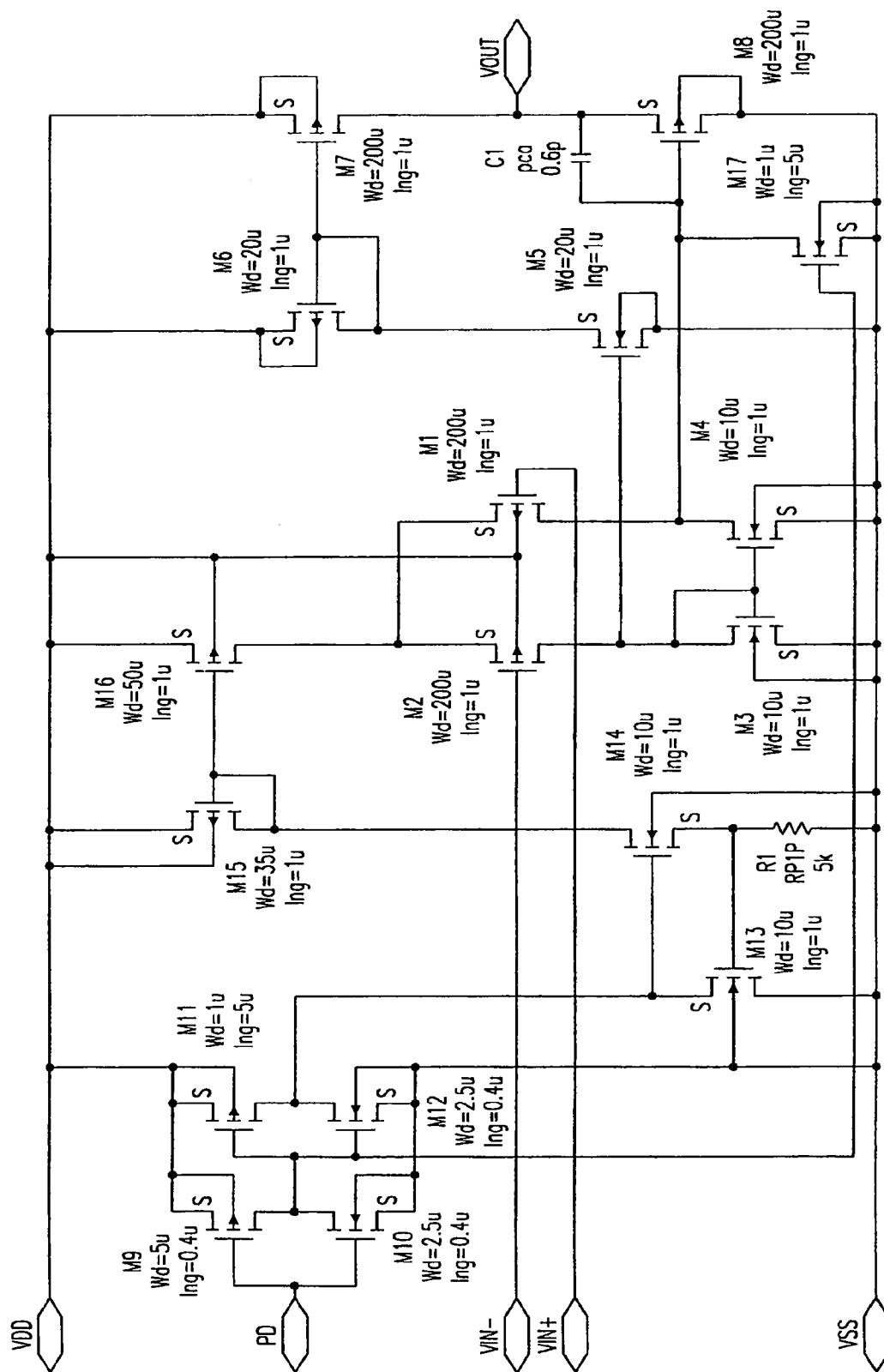


FIG. 111

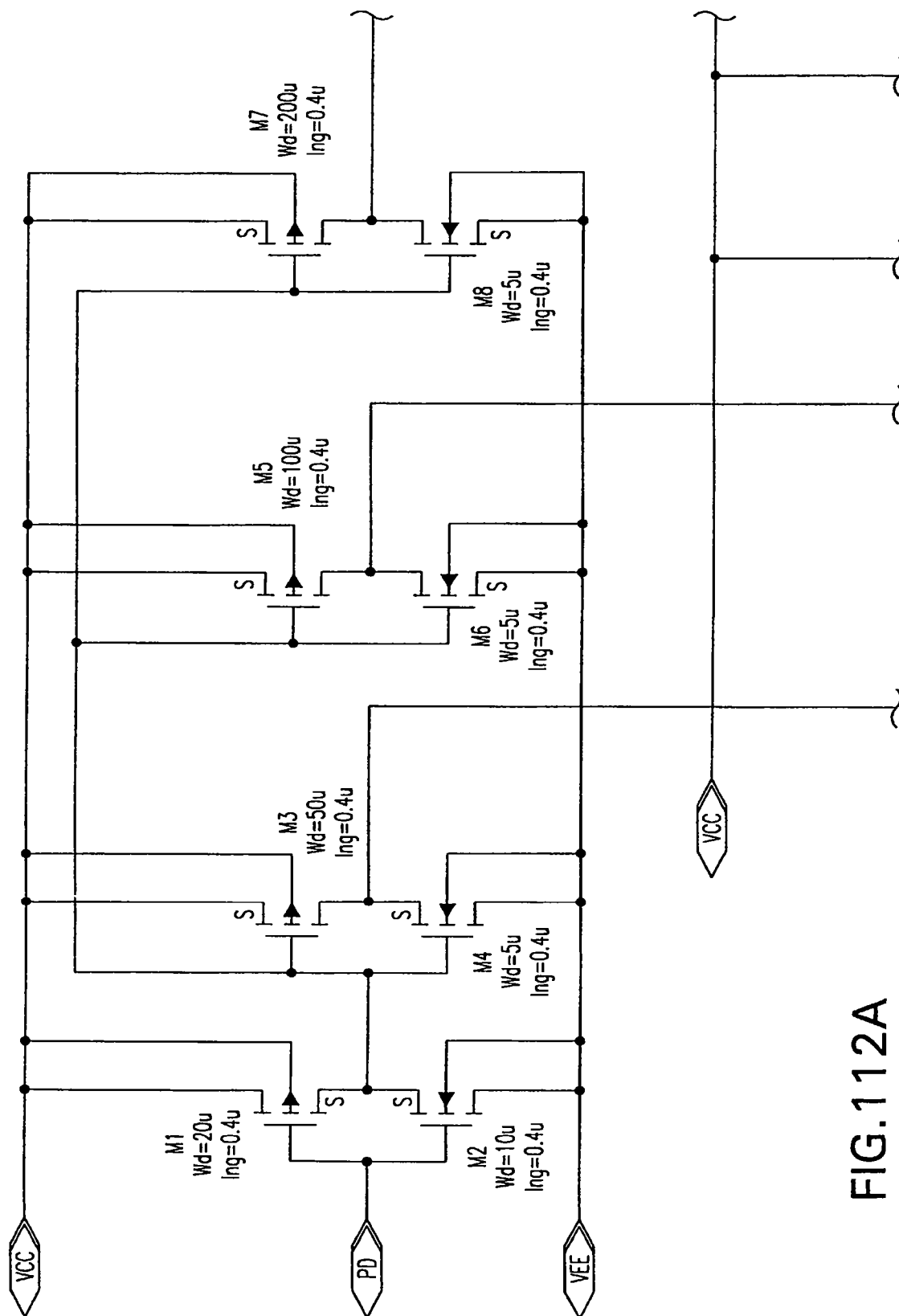
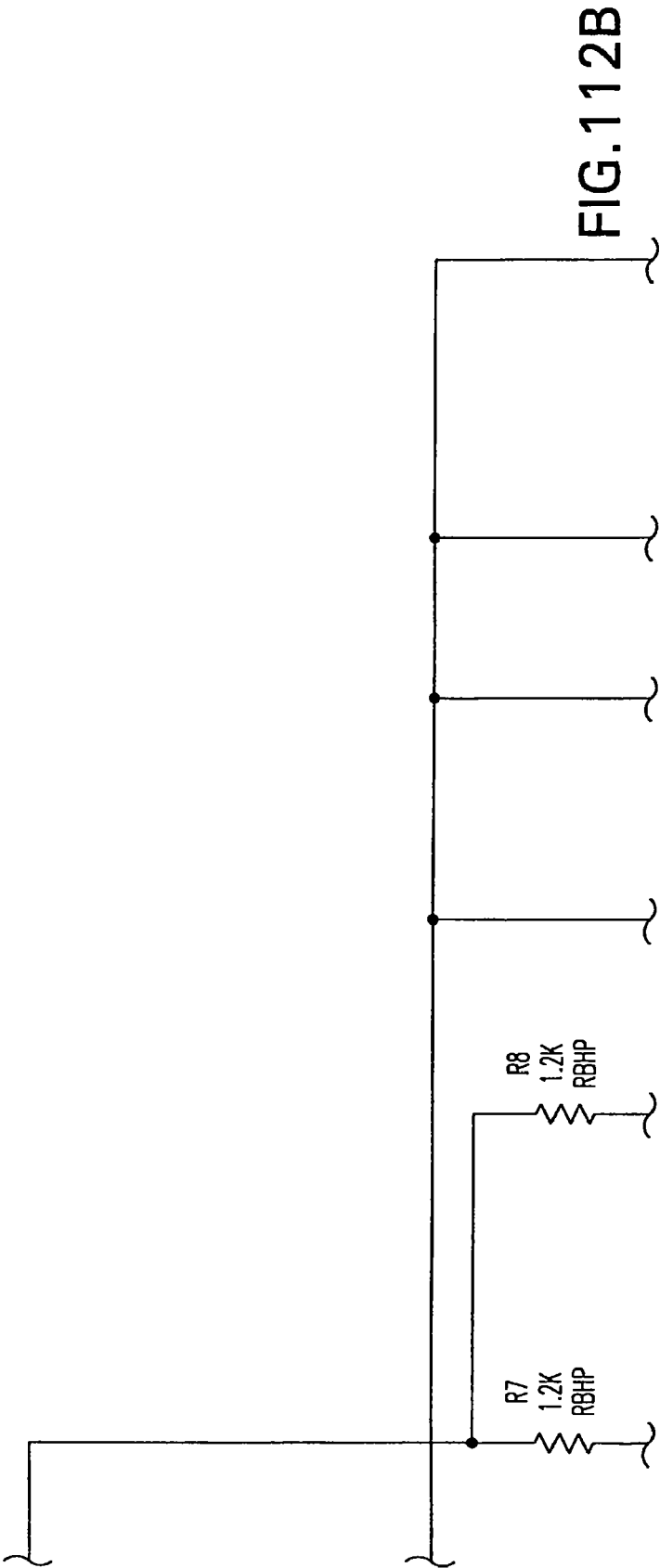


FIG. 112A



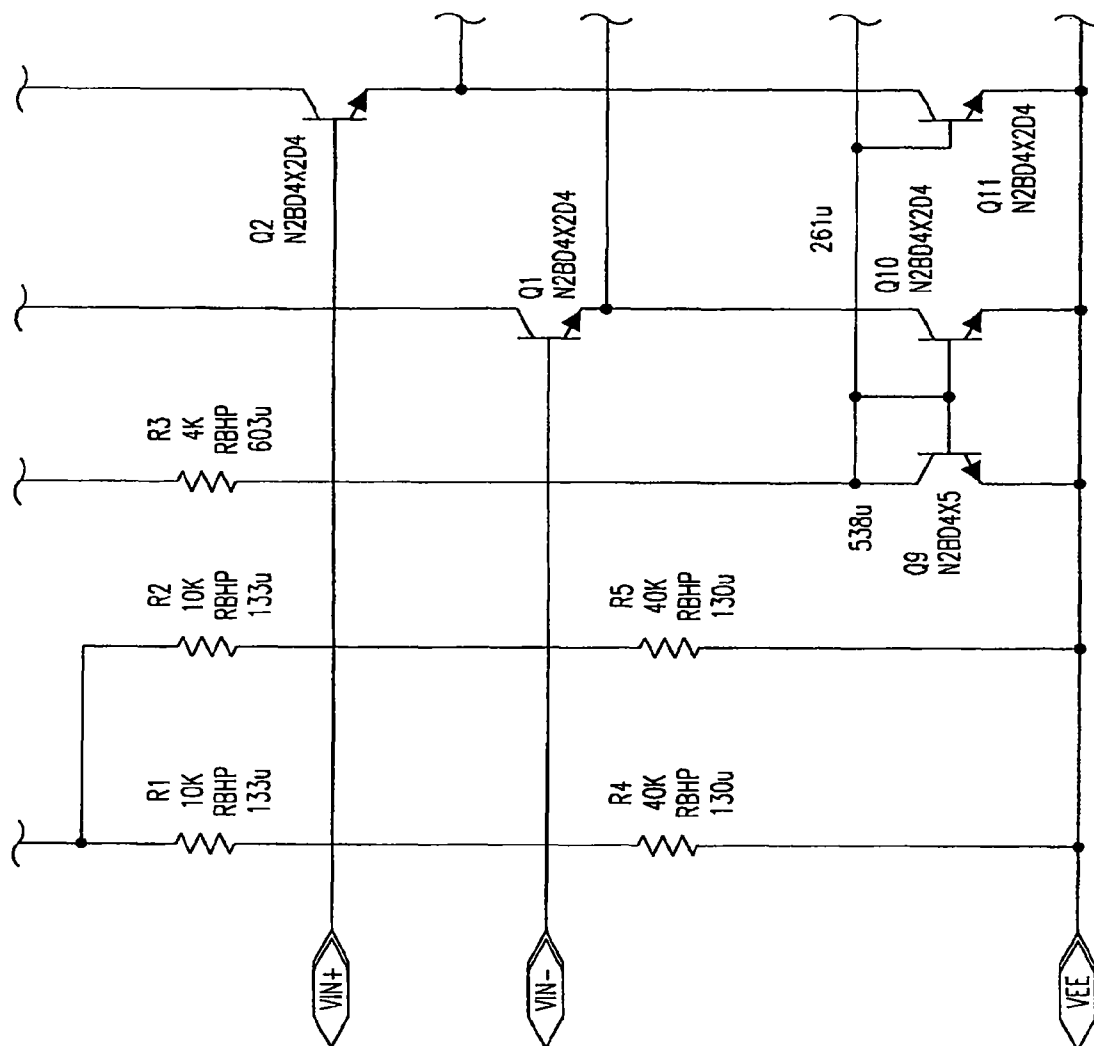
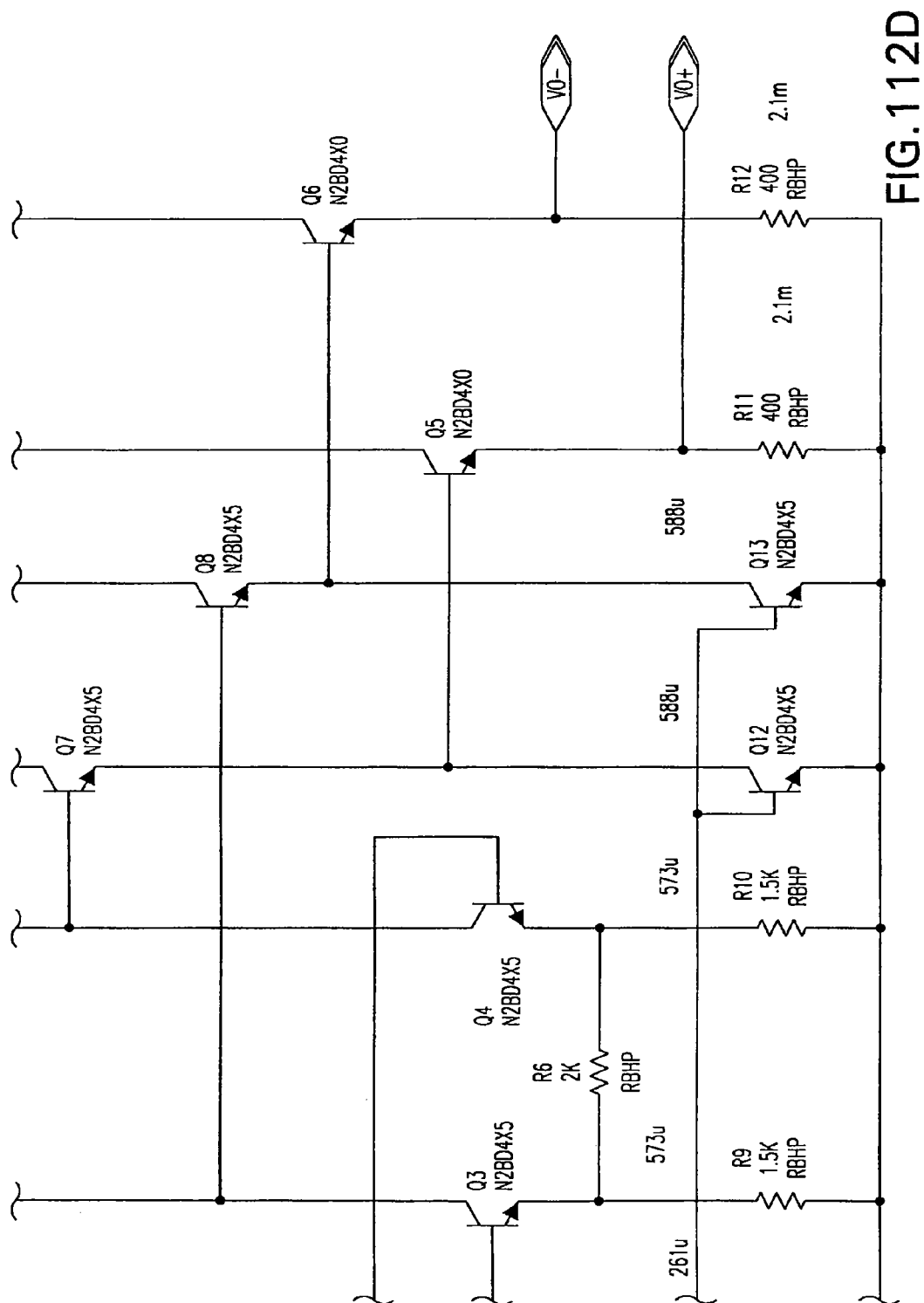


FIG. 112C



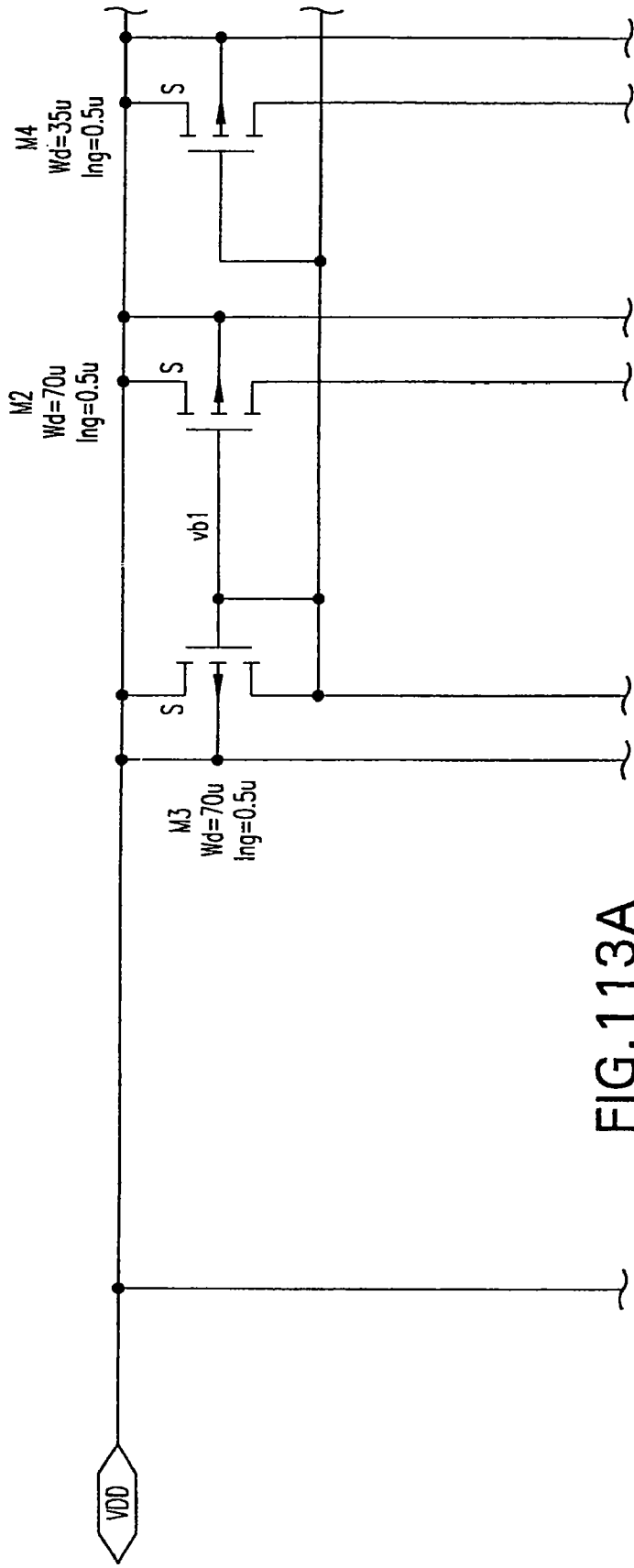


FIG.113A

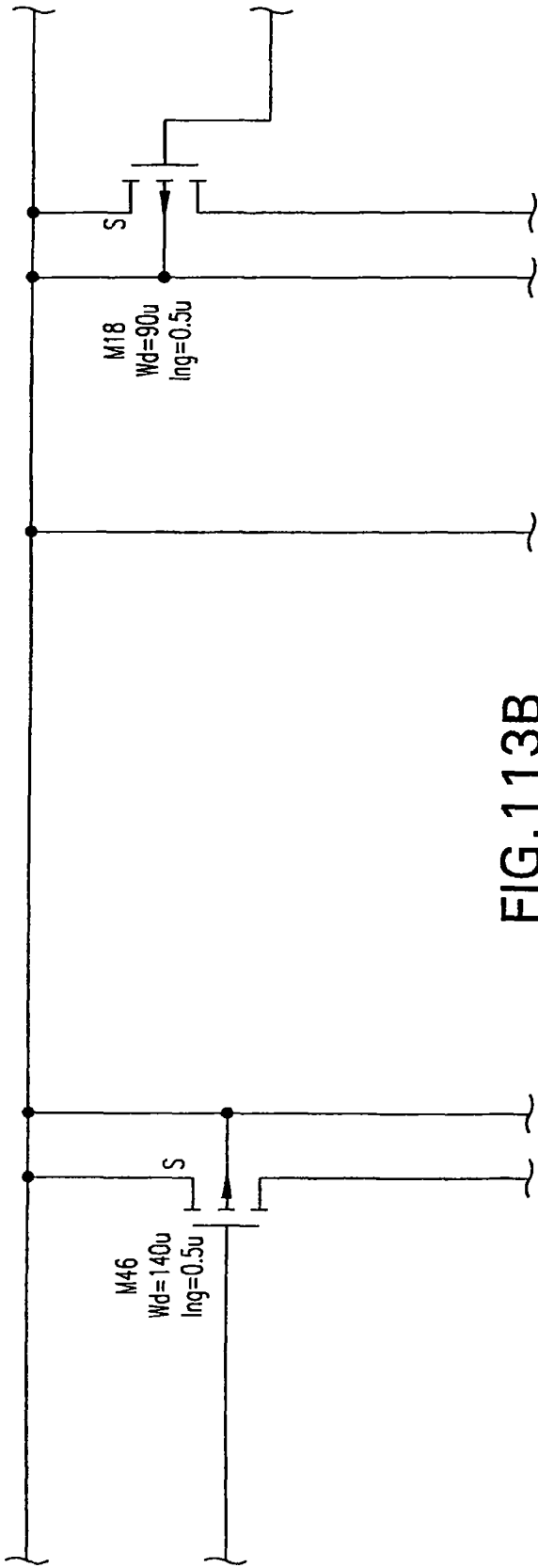


FIG.113B

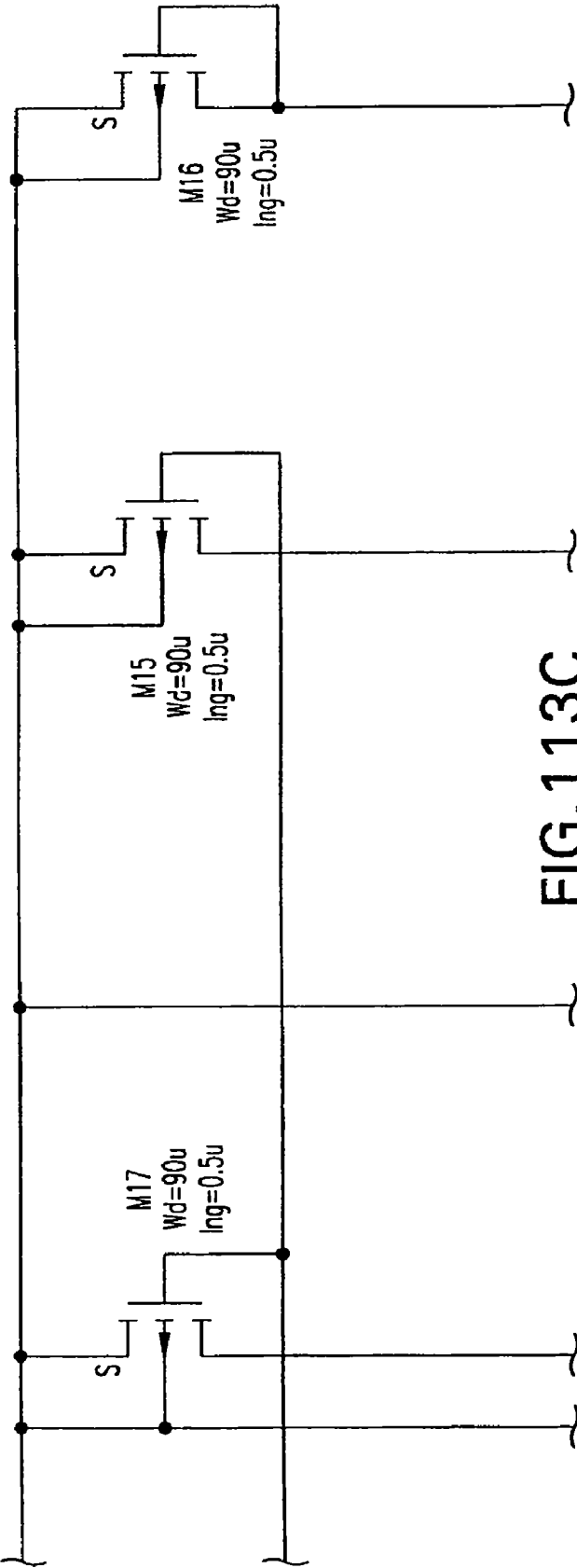
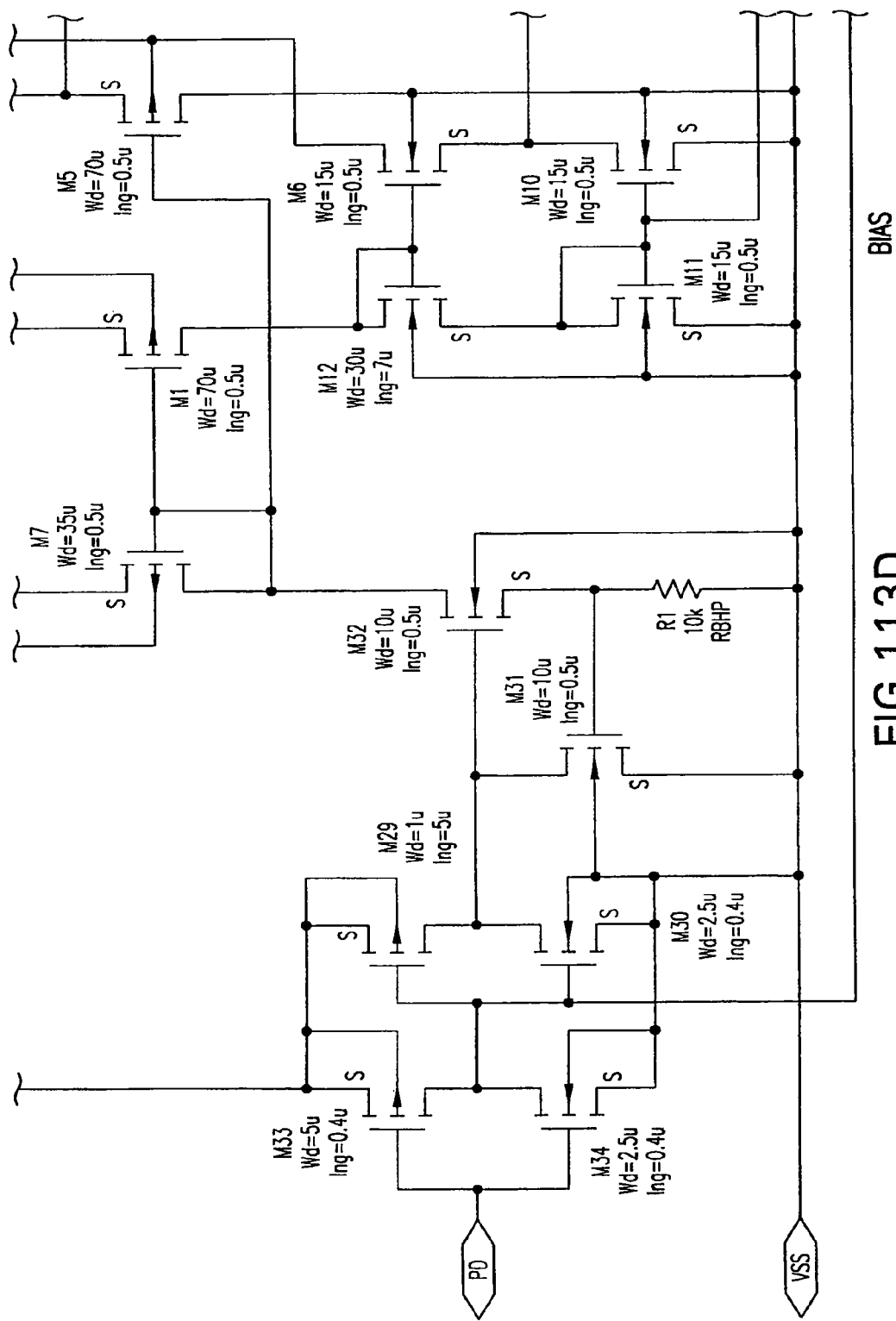


FIG. 113C





BIAS

FIG.113D

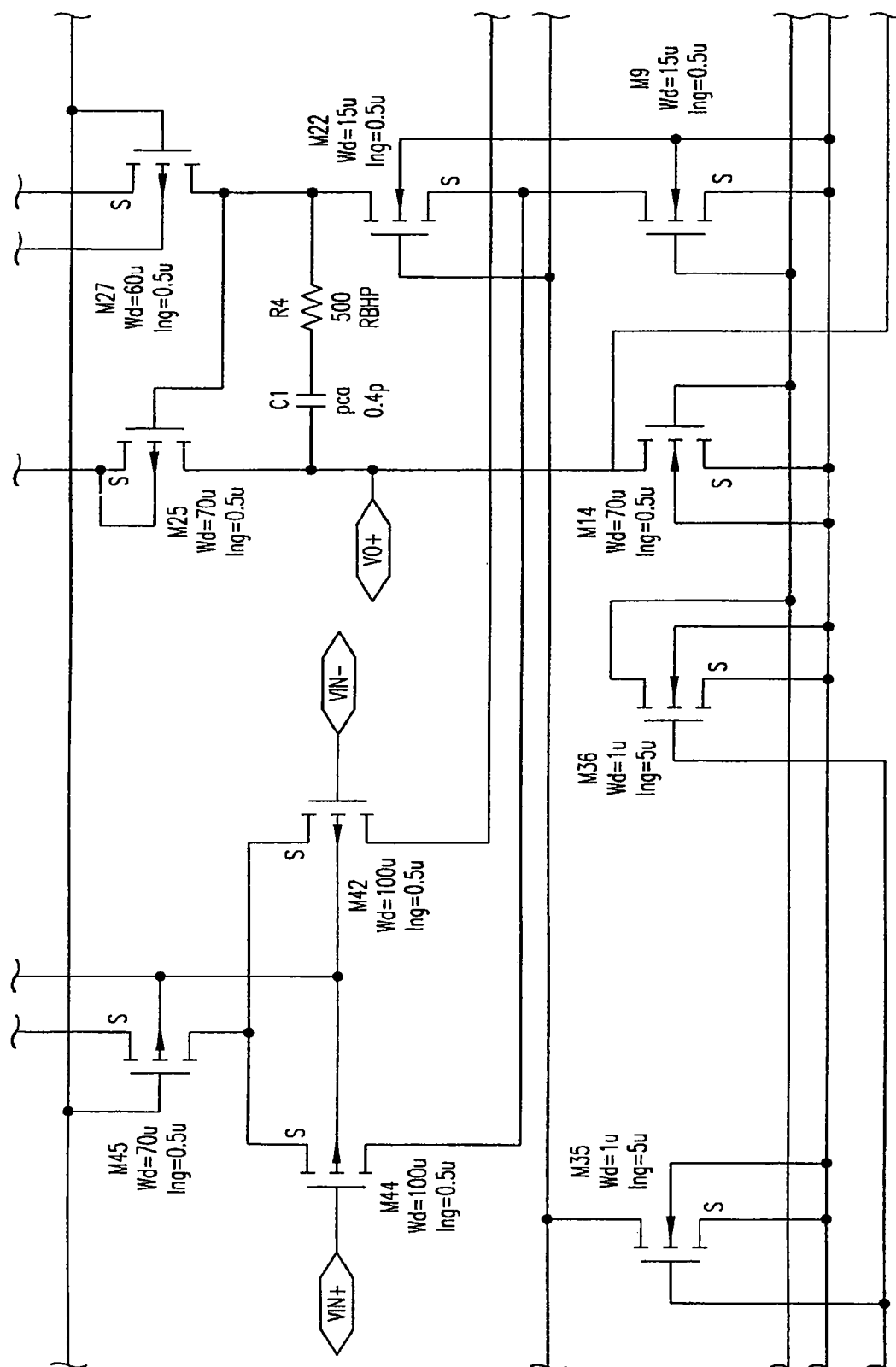


FIG. 113E

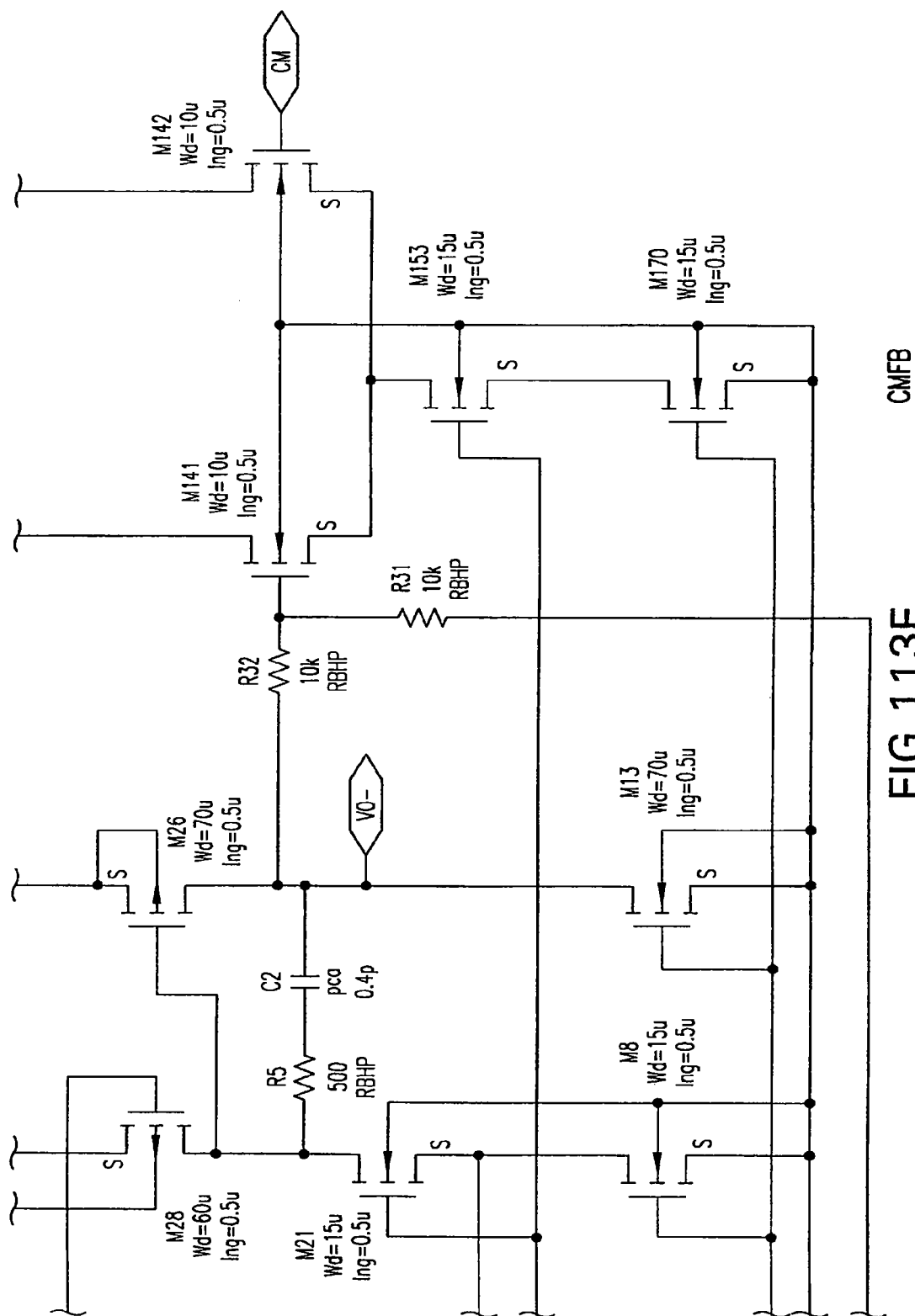


FIG. 13F

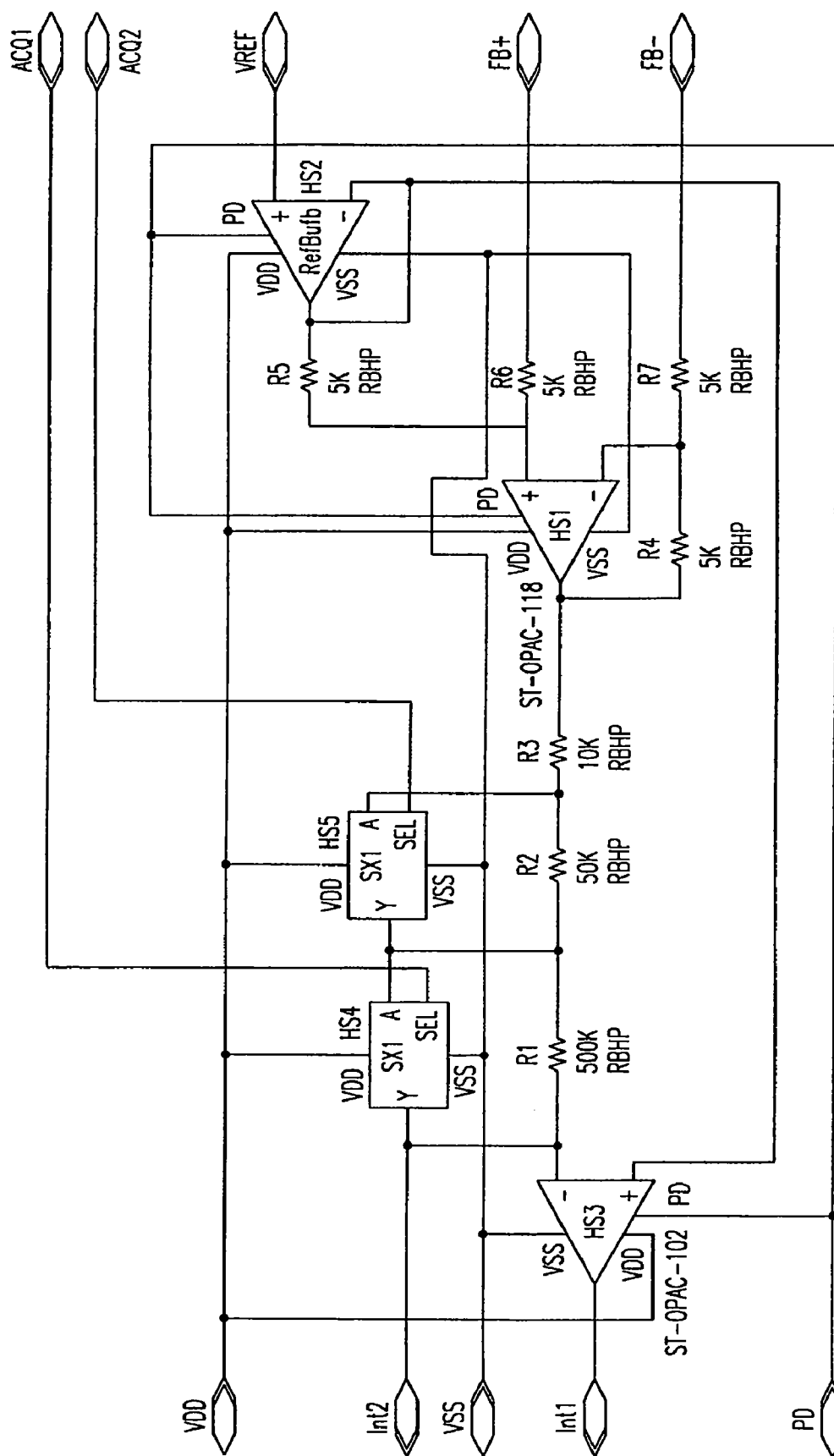


FIG. 114

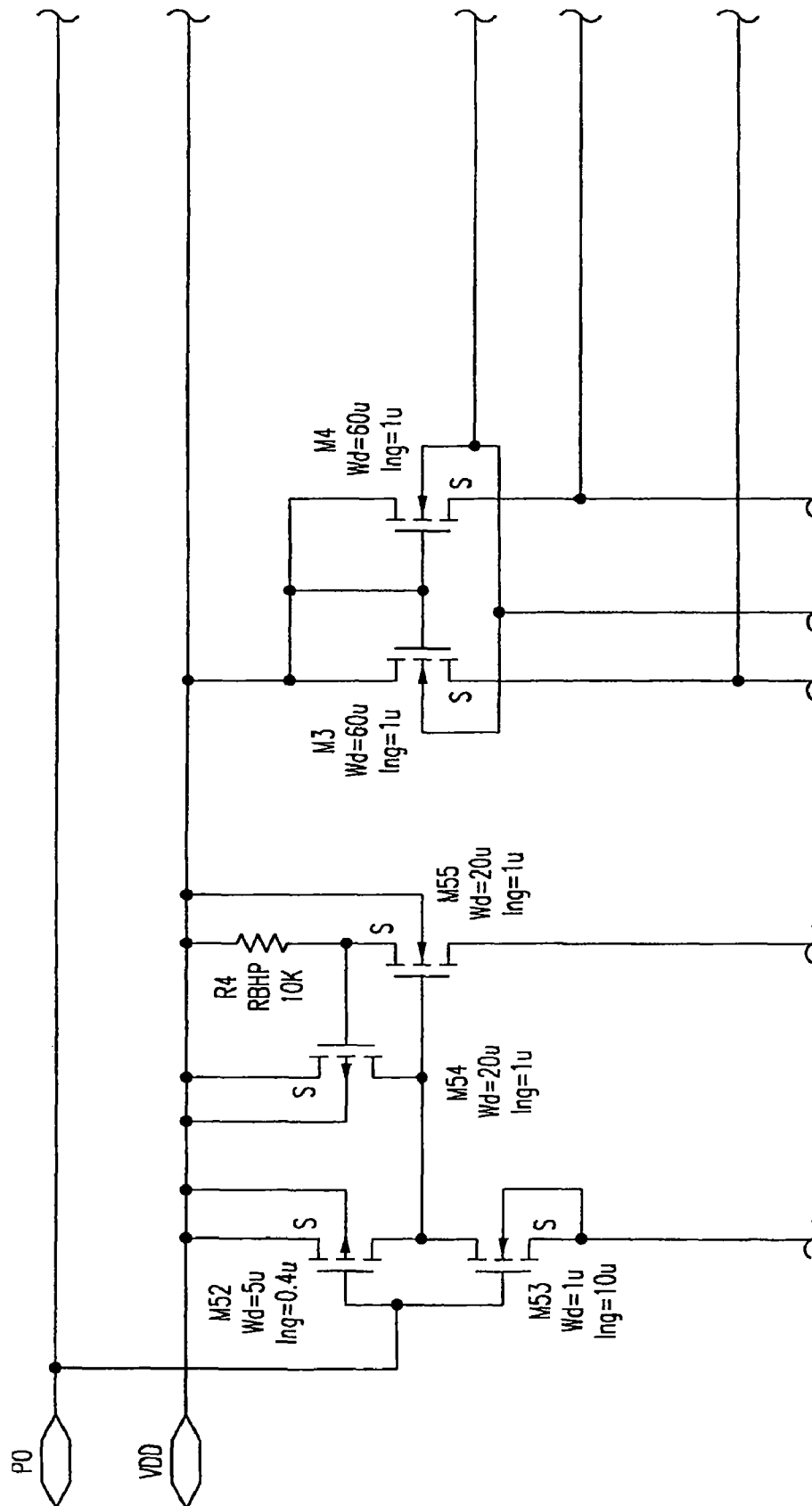


FIG. 115A

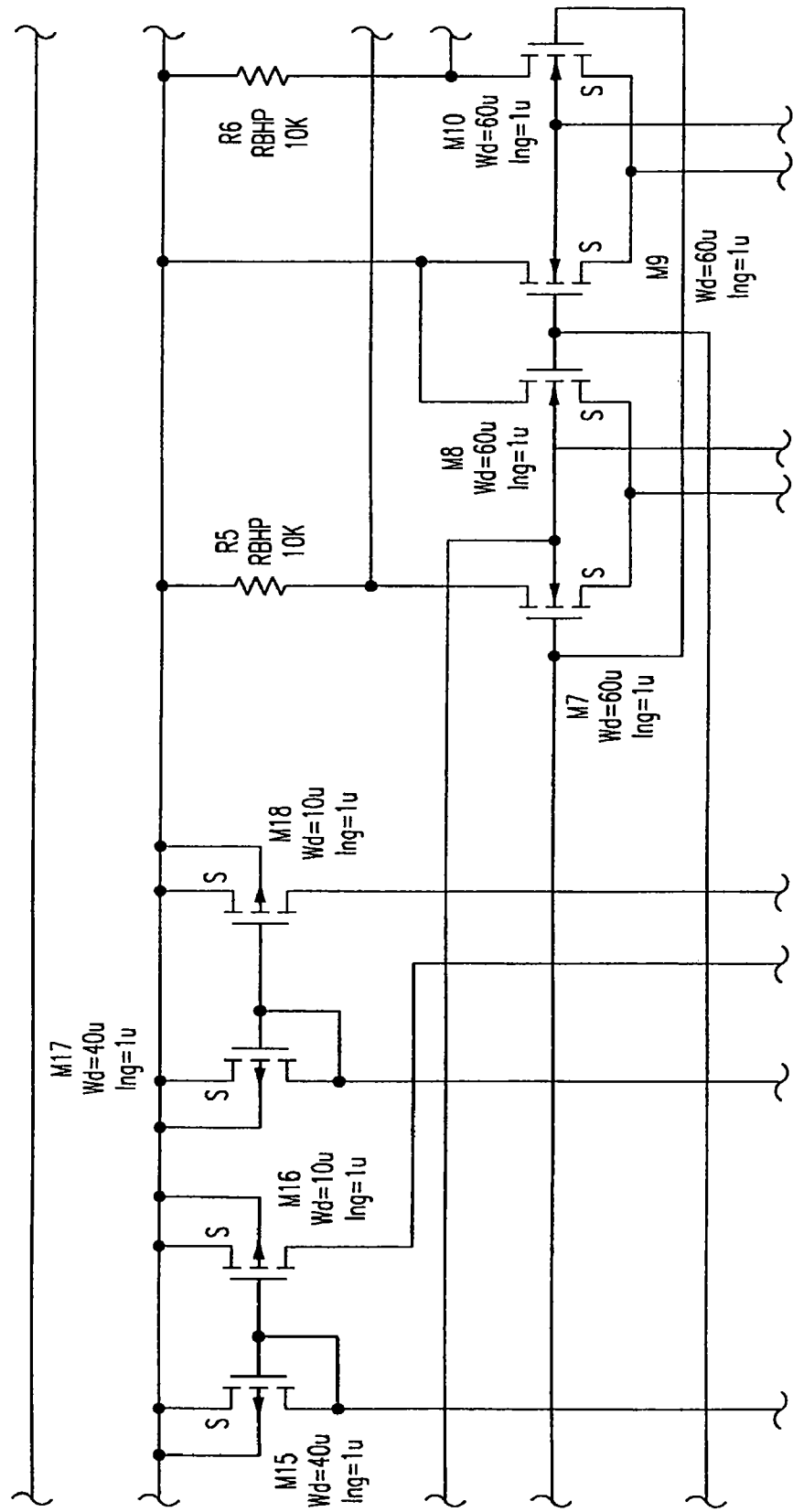


FIG. 115B

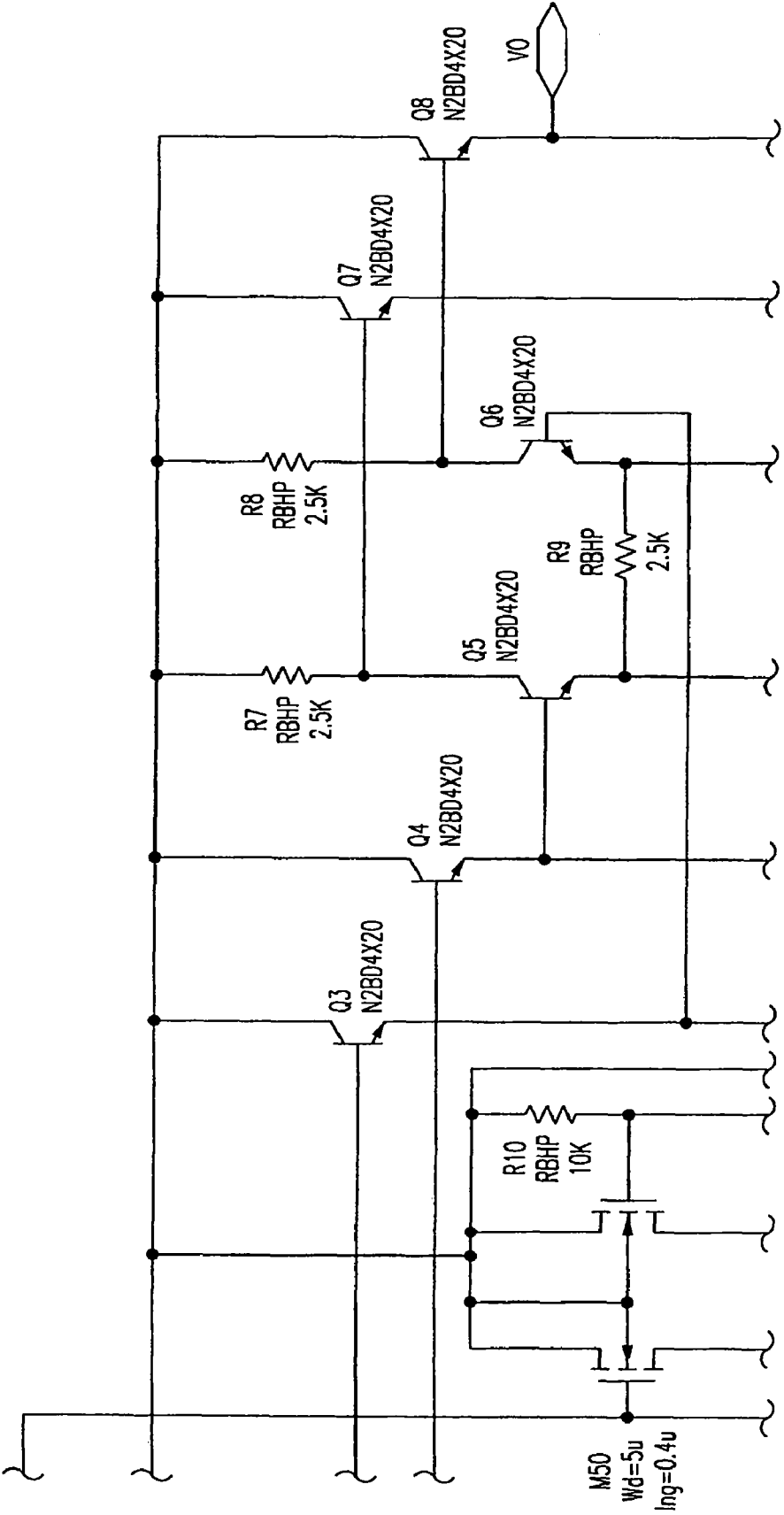


FIG. 115C

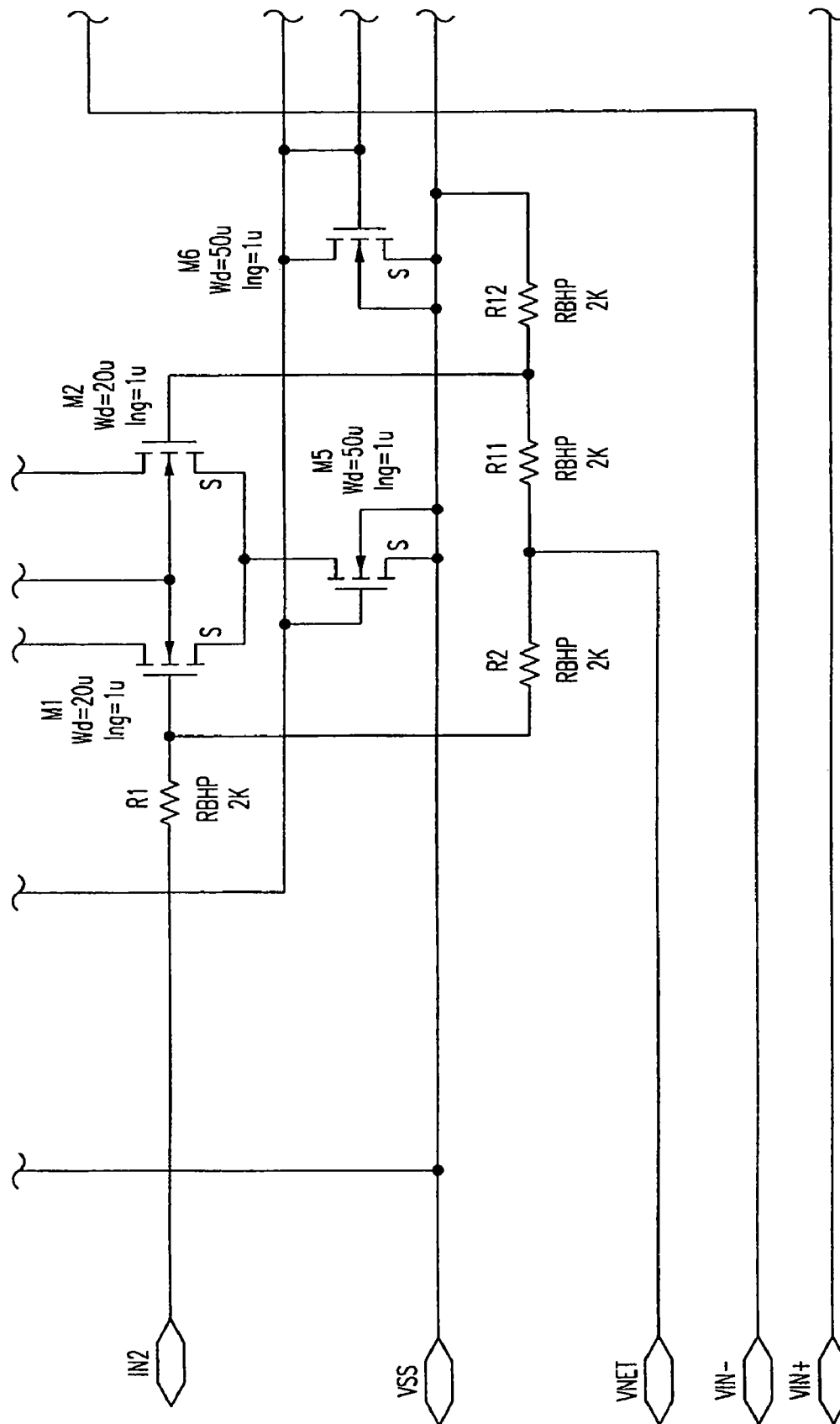
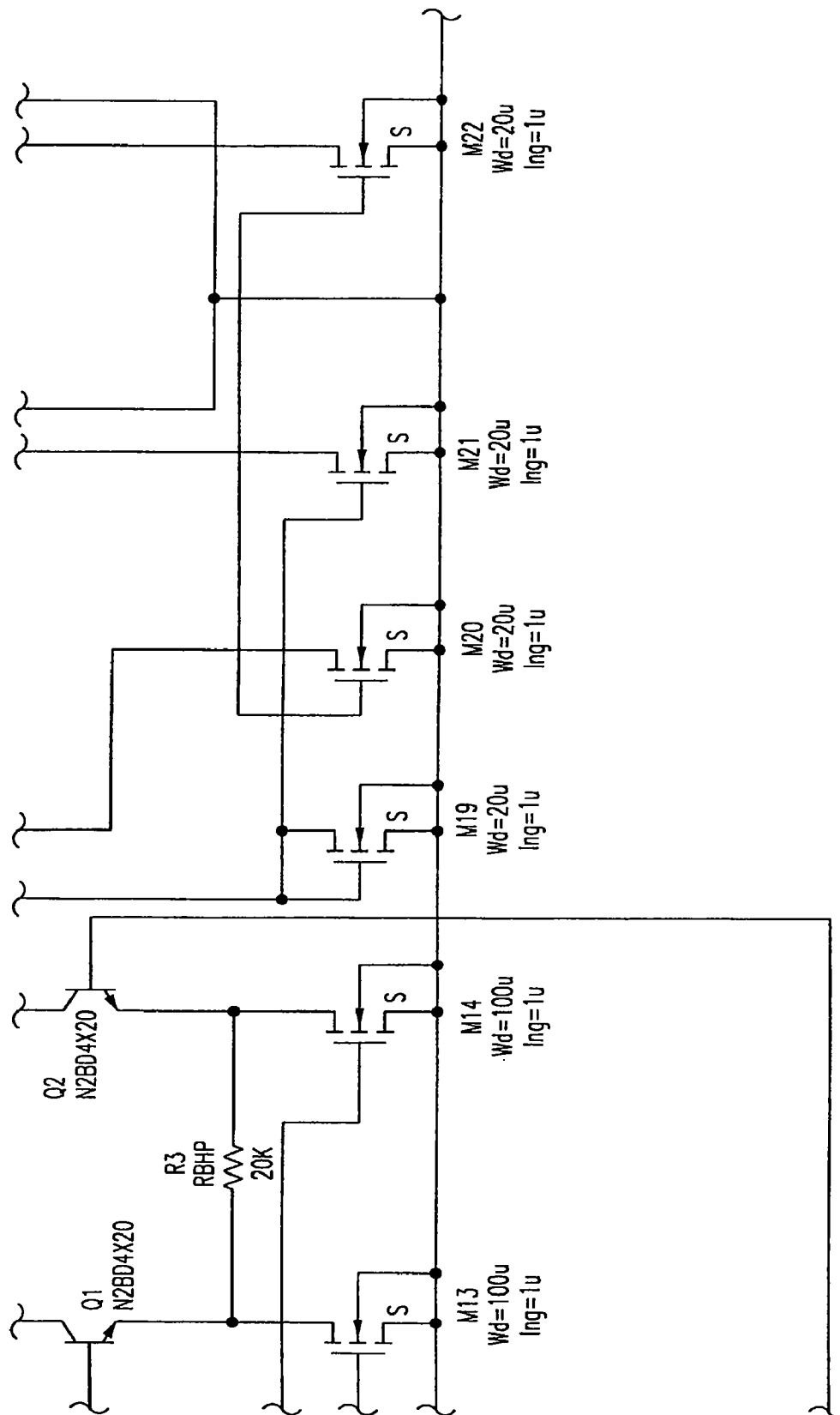


FIG. 115D





**FIG. 115E**

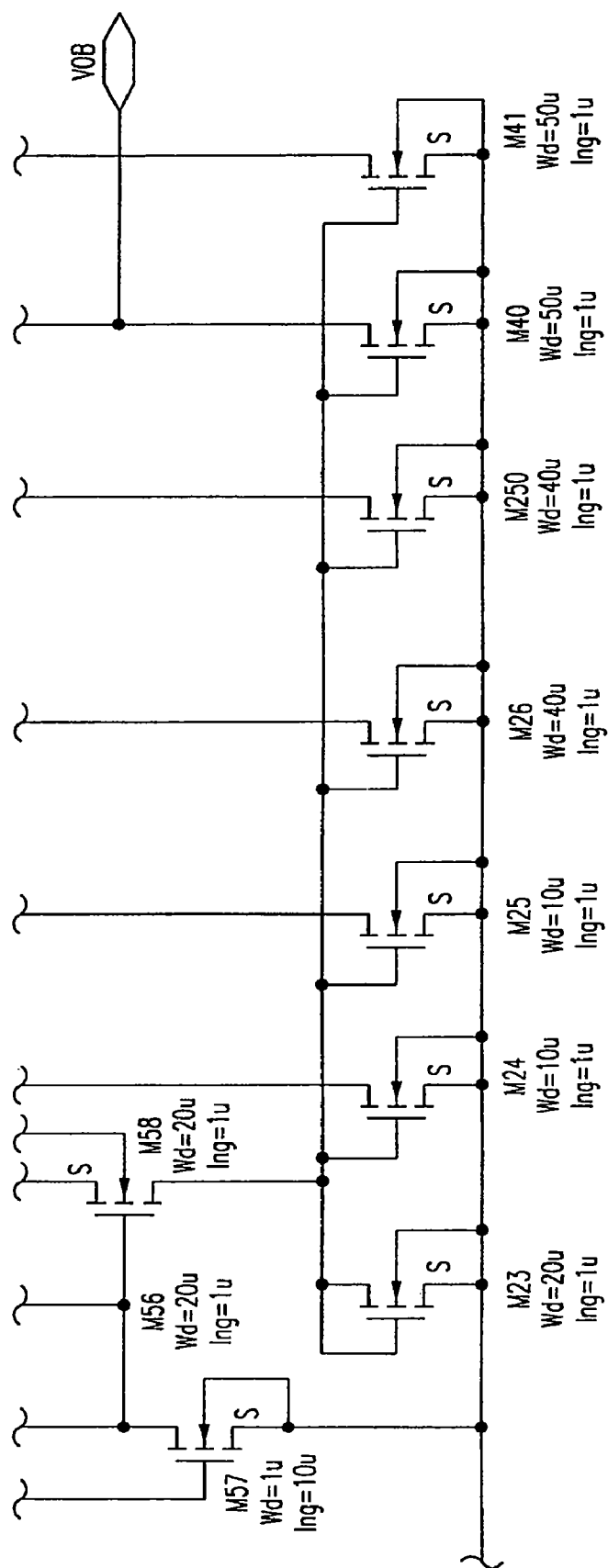


FIG. 115F

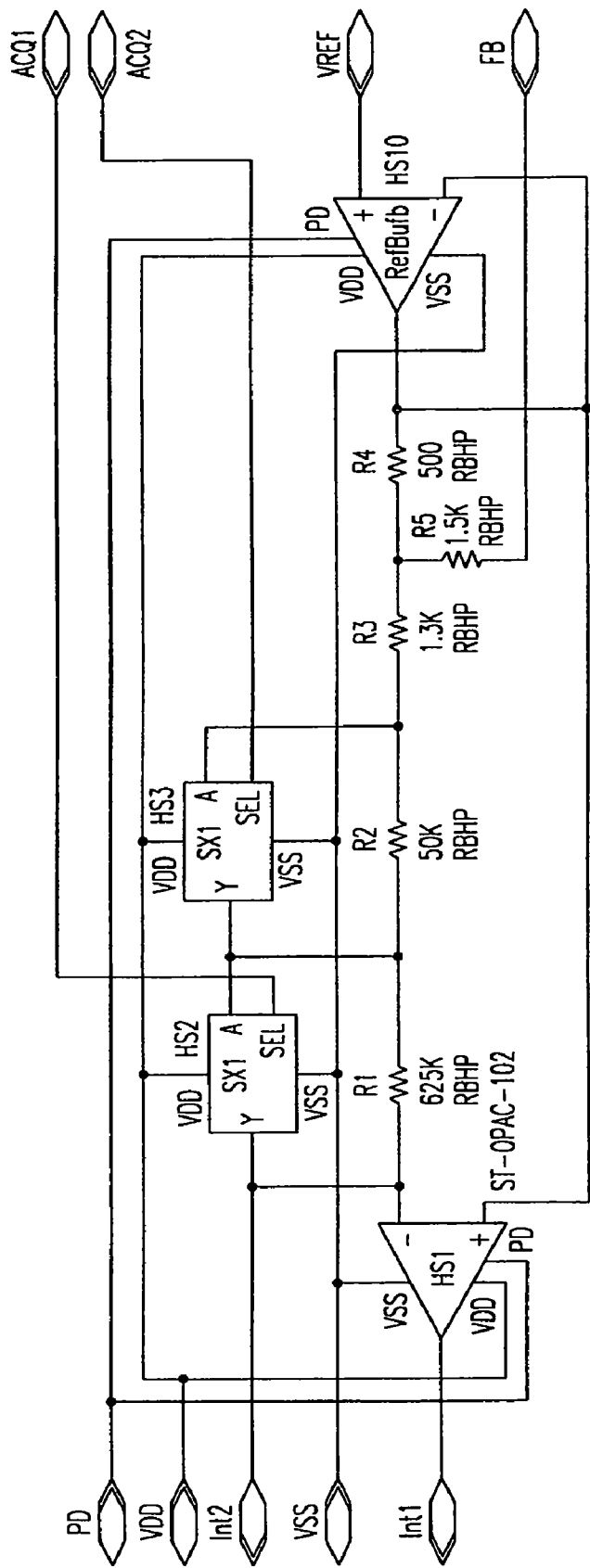


FIG.116

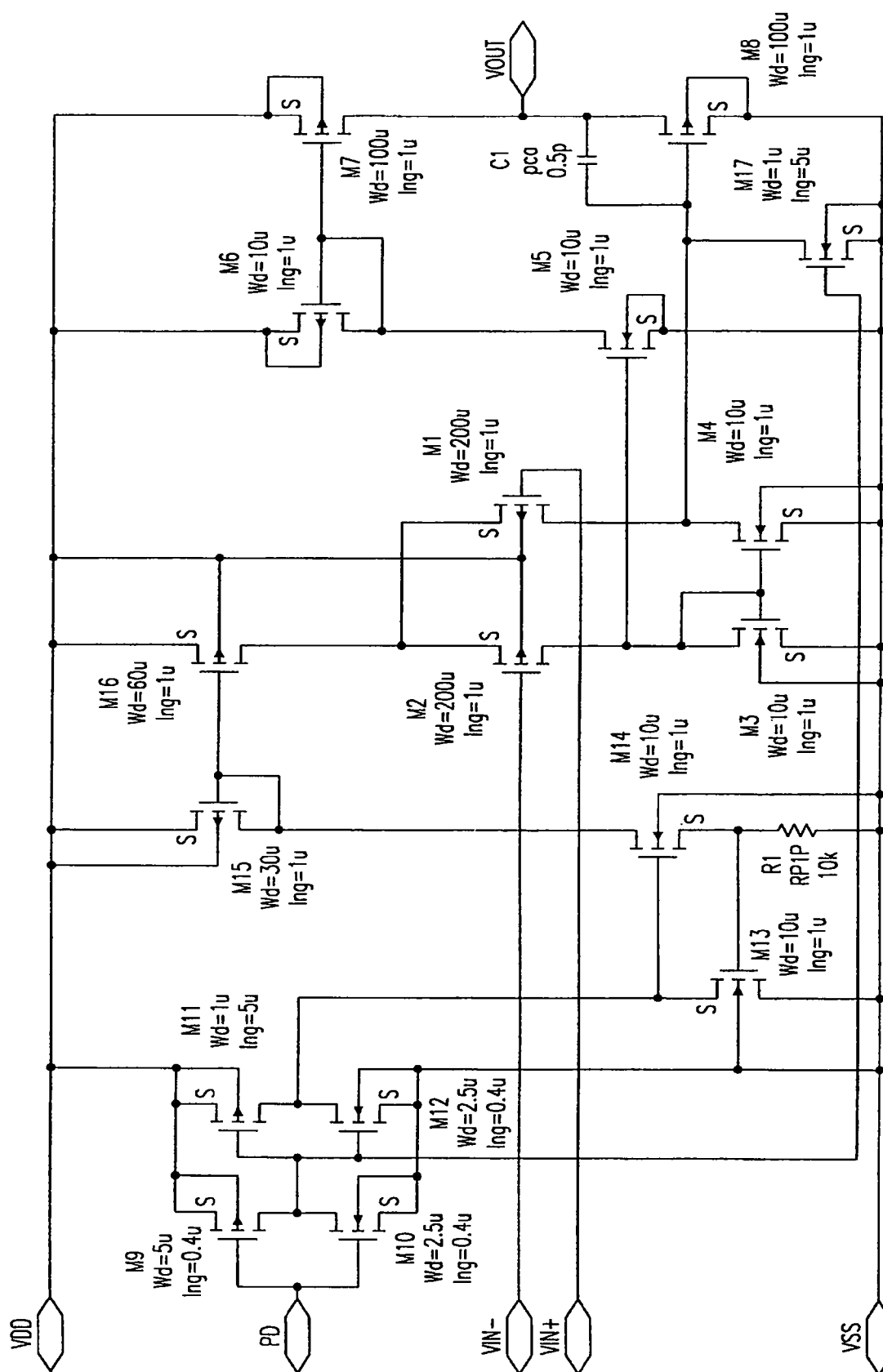


FIG. 117

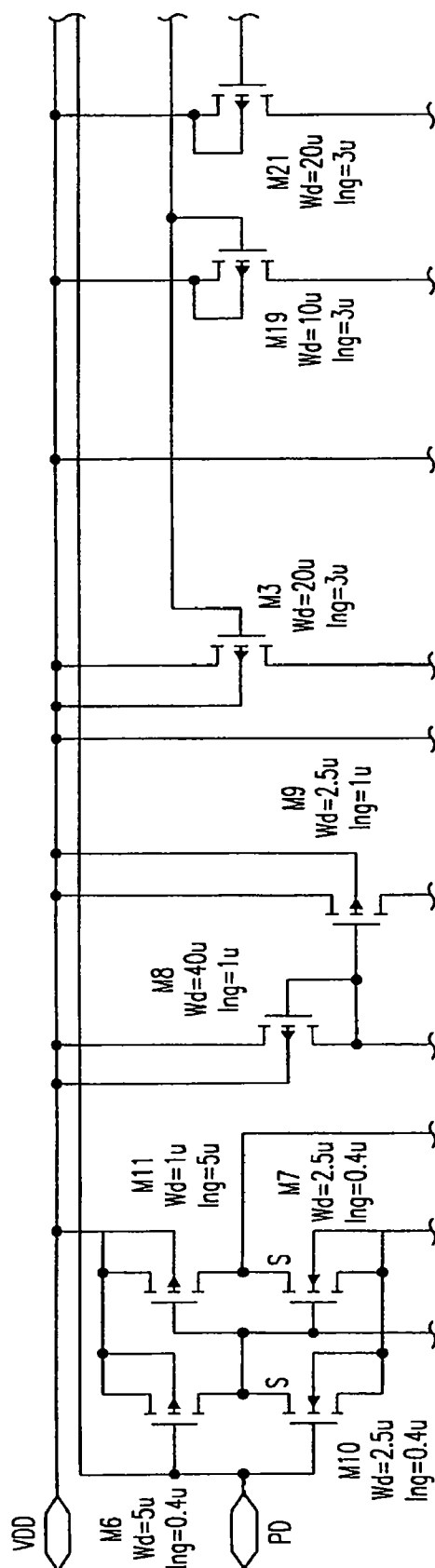


FIG. 118A

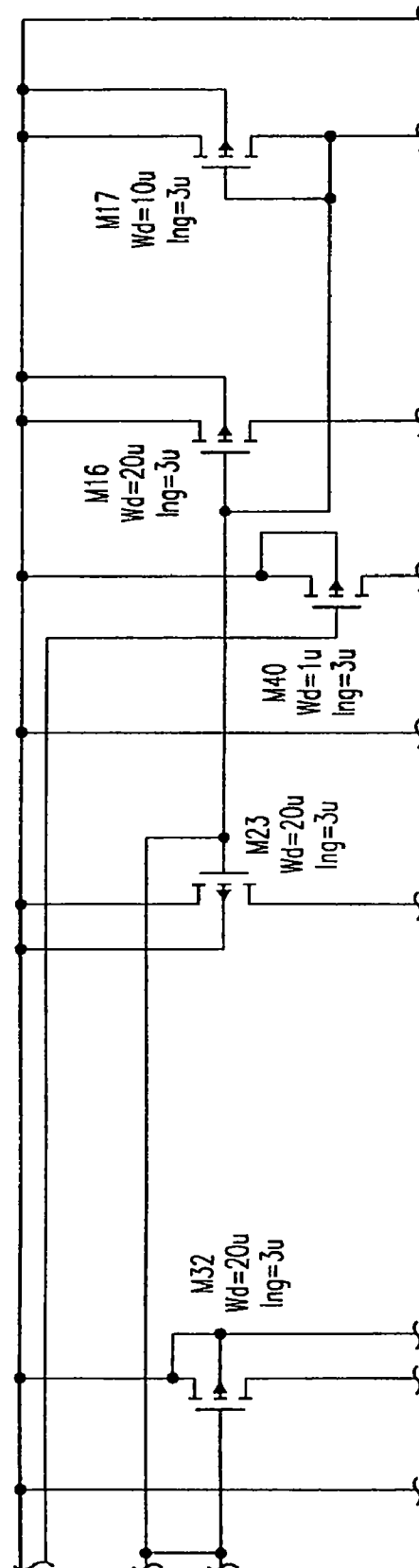


FIG. 118B

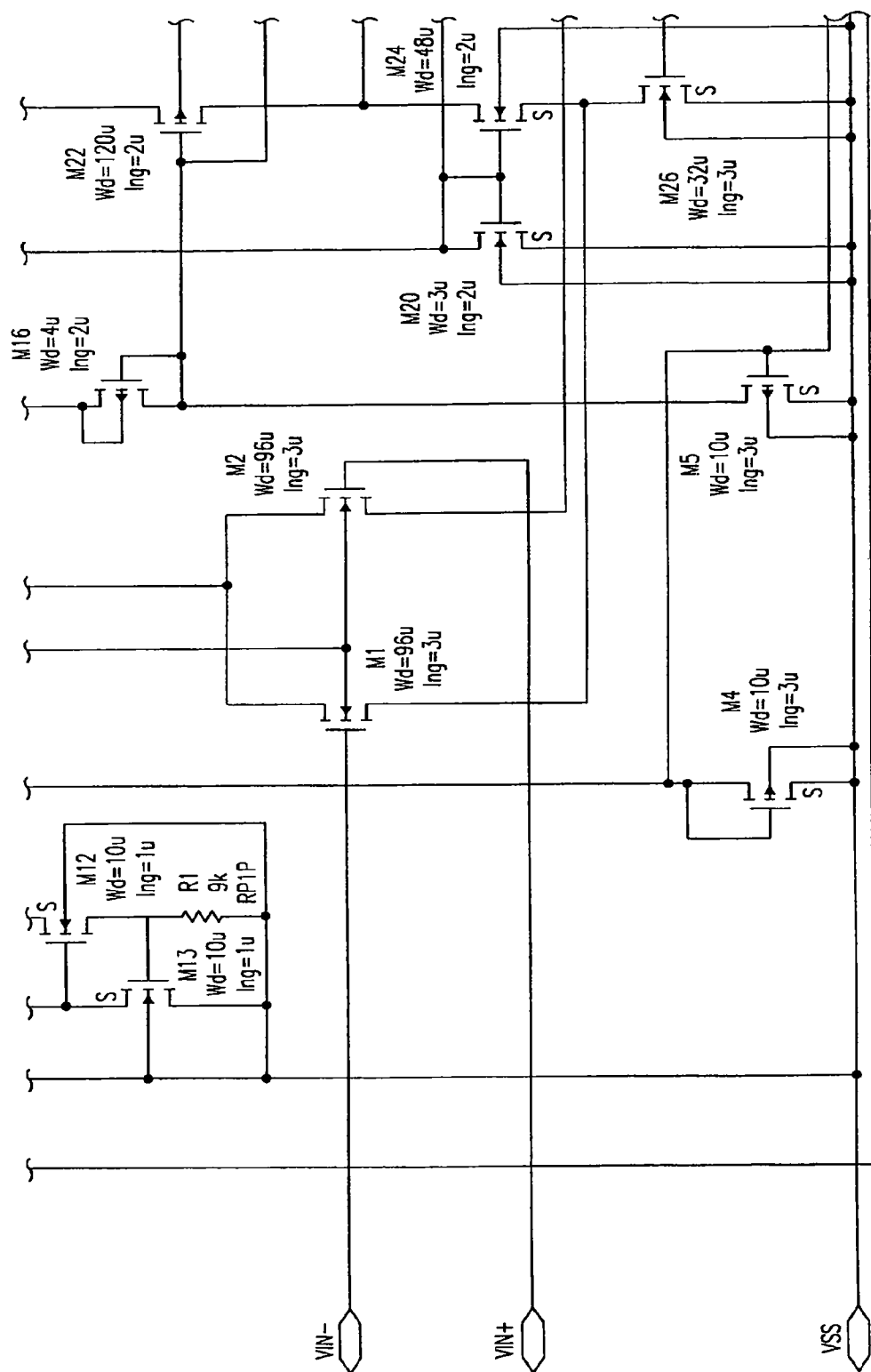


FIG. 118C

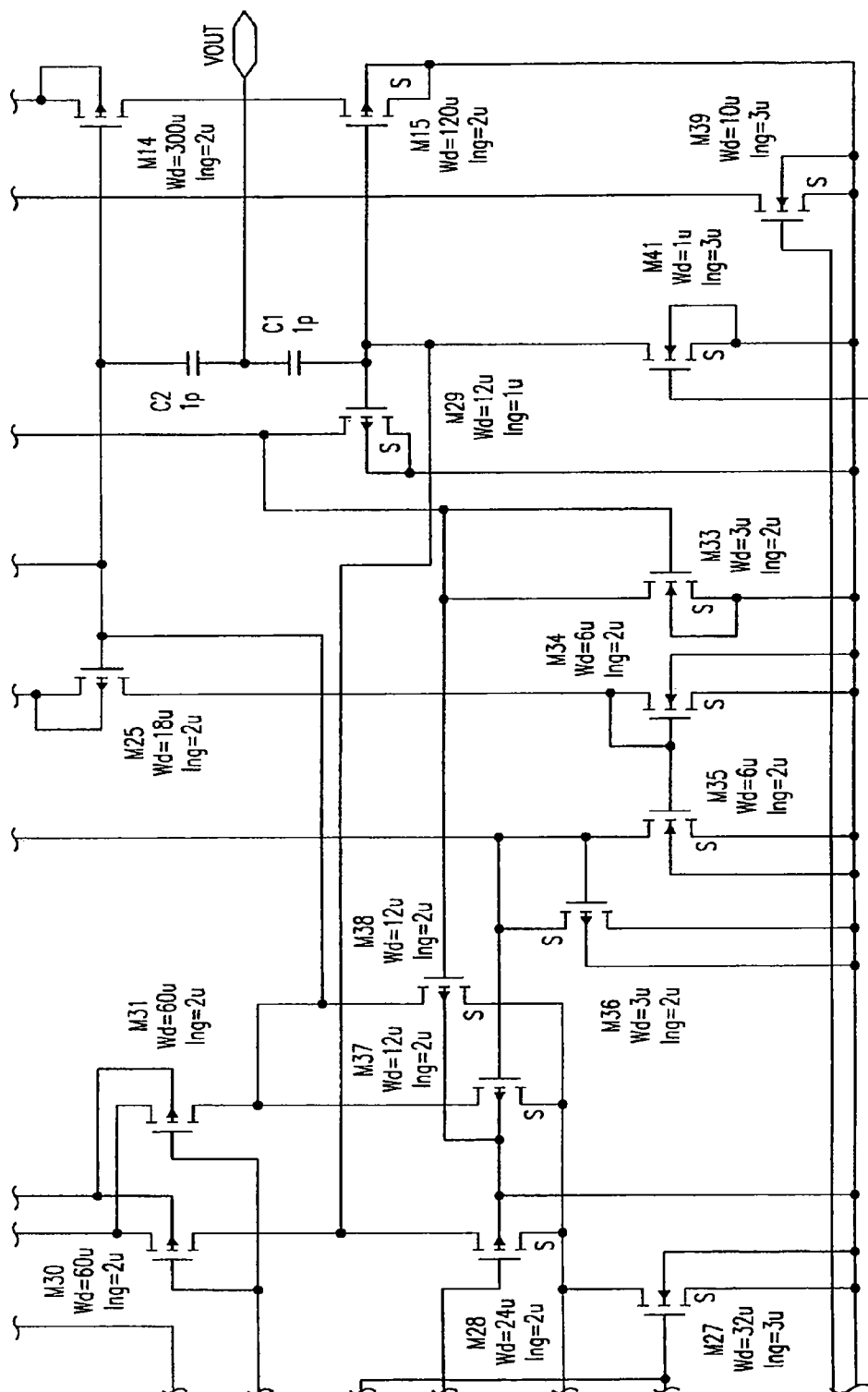
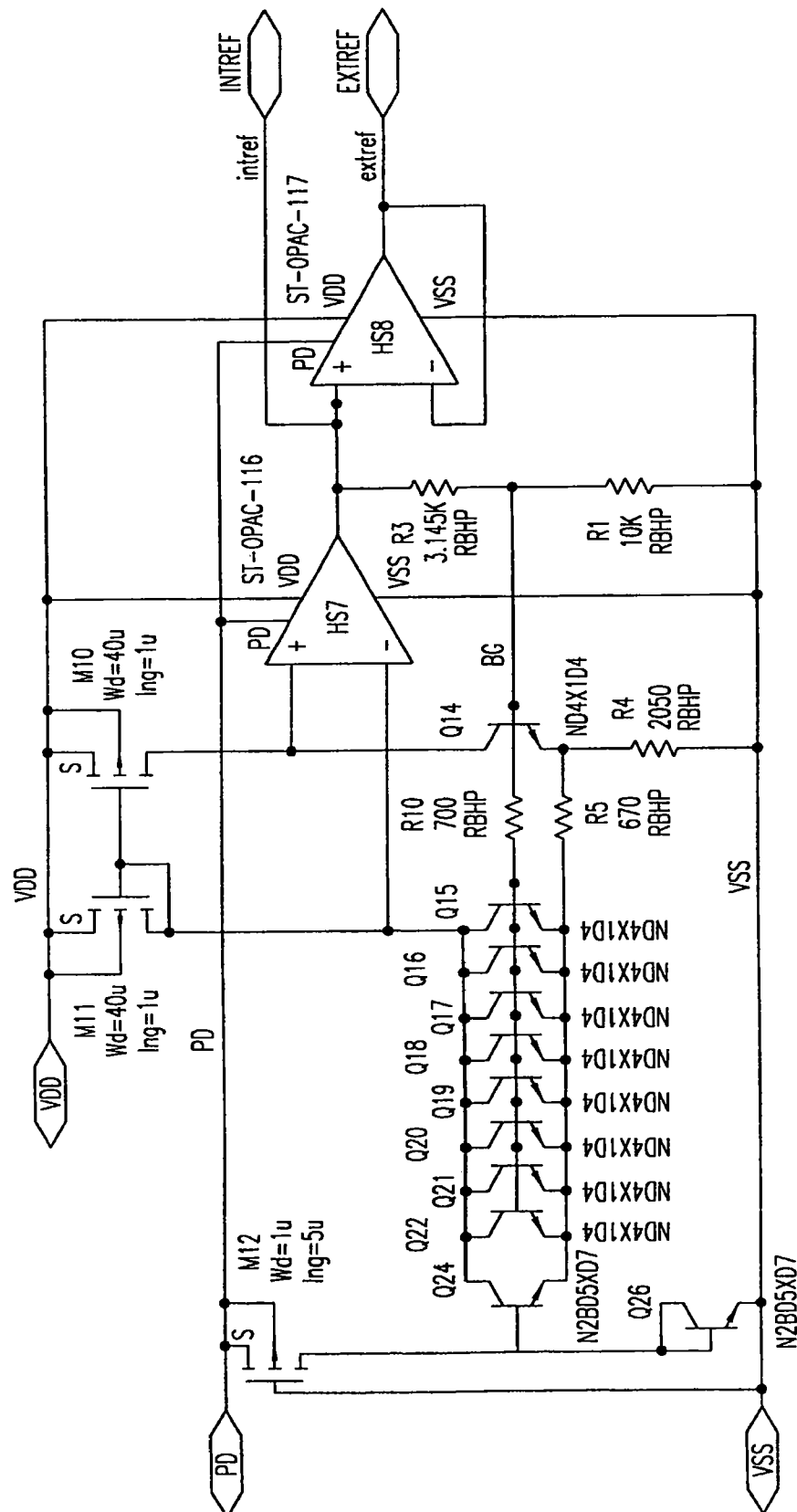


FIG. 118D





**FIG. 119**

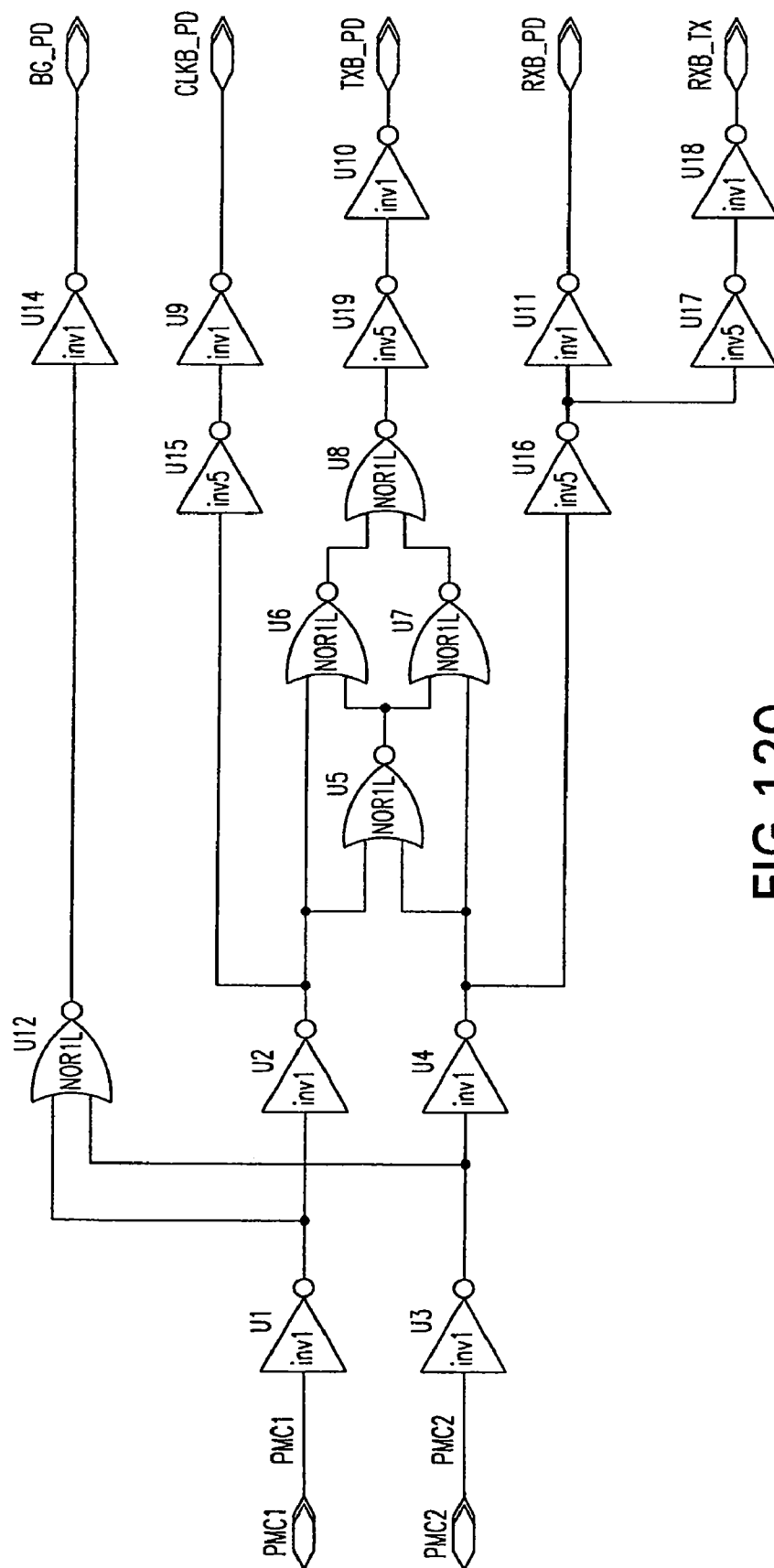


FIG. 120

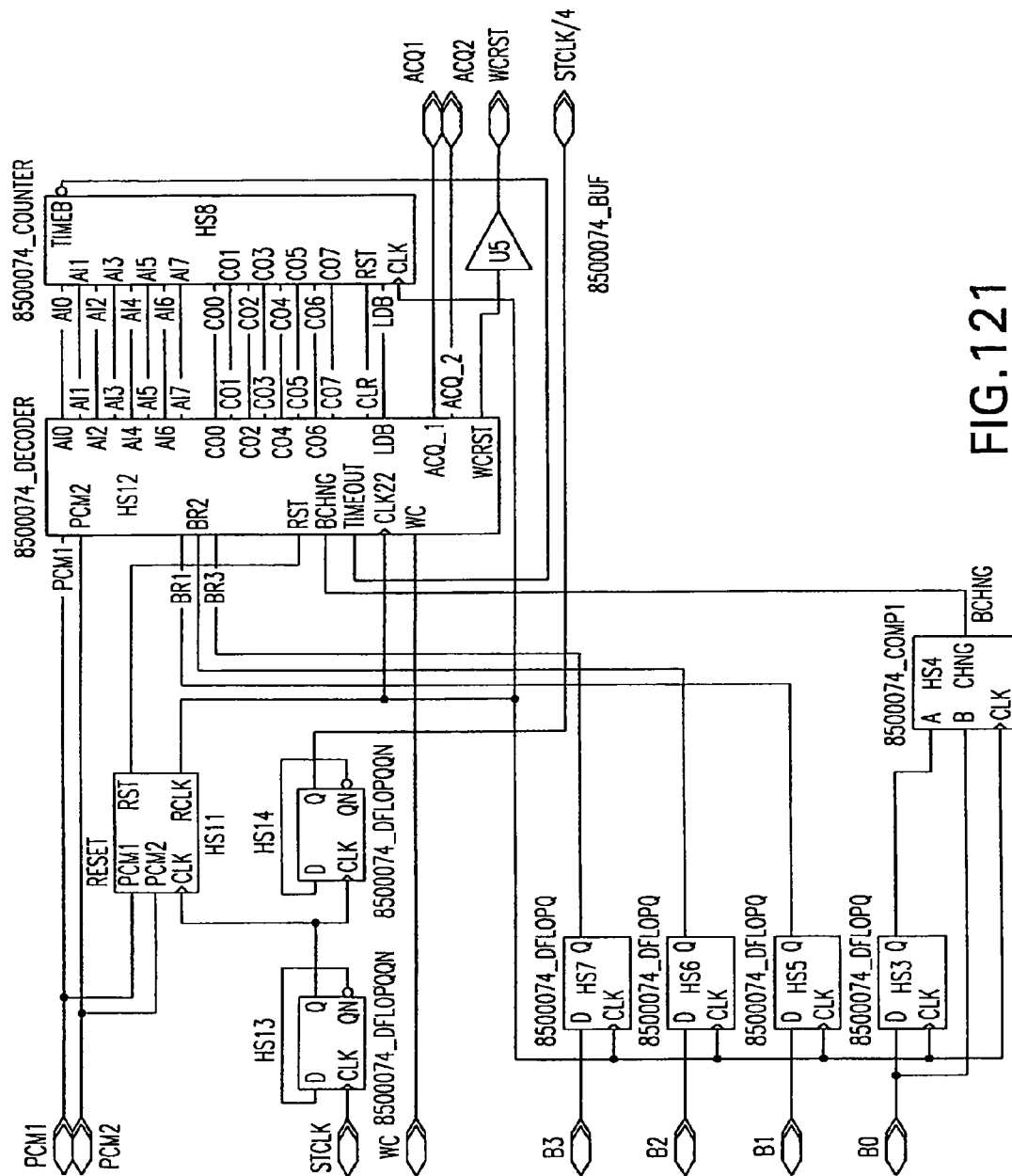


FIG. 121

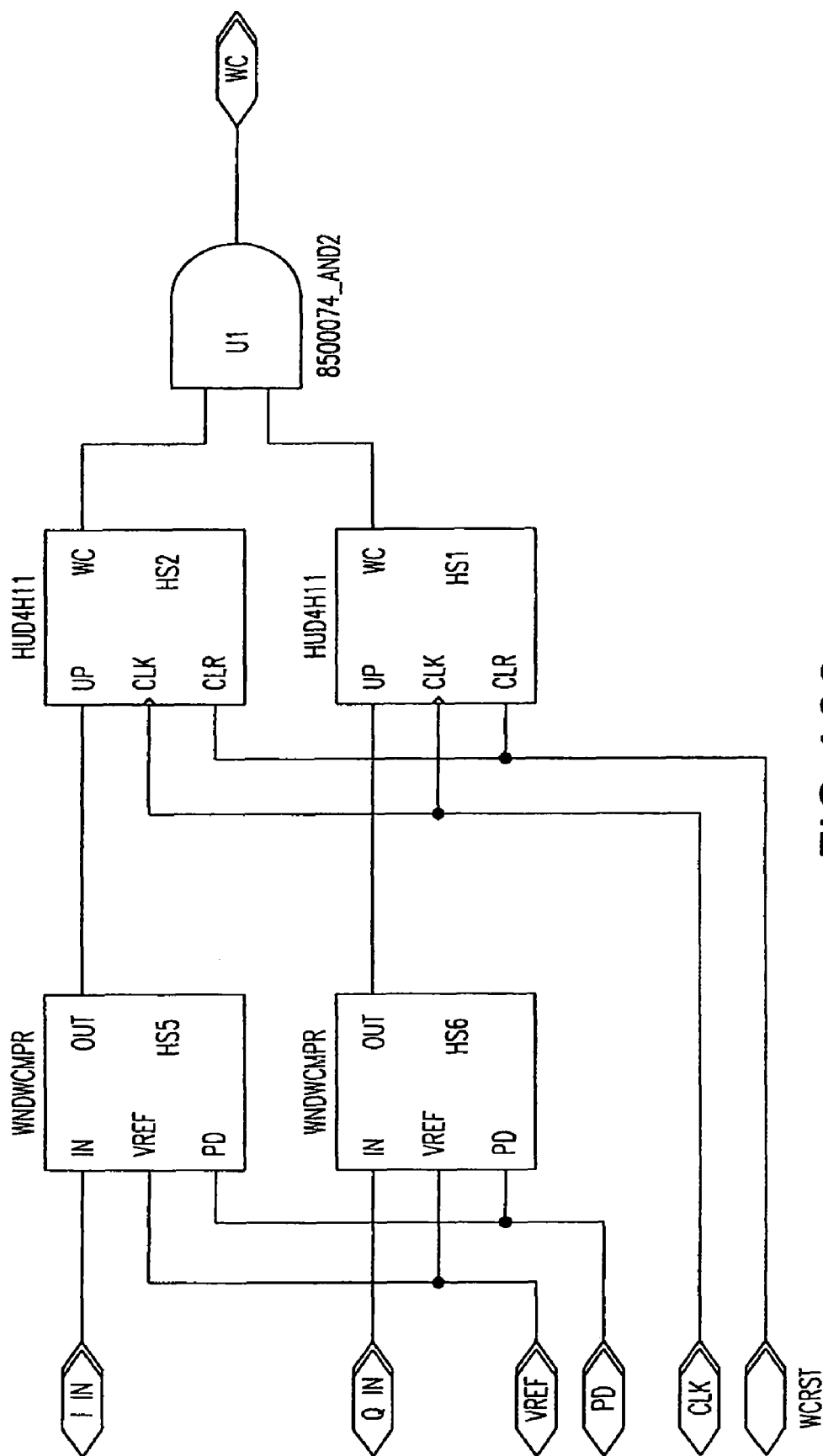


FIG. 122

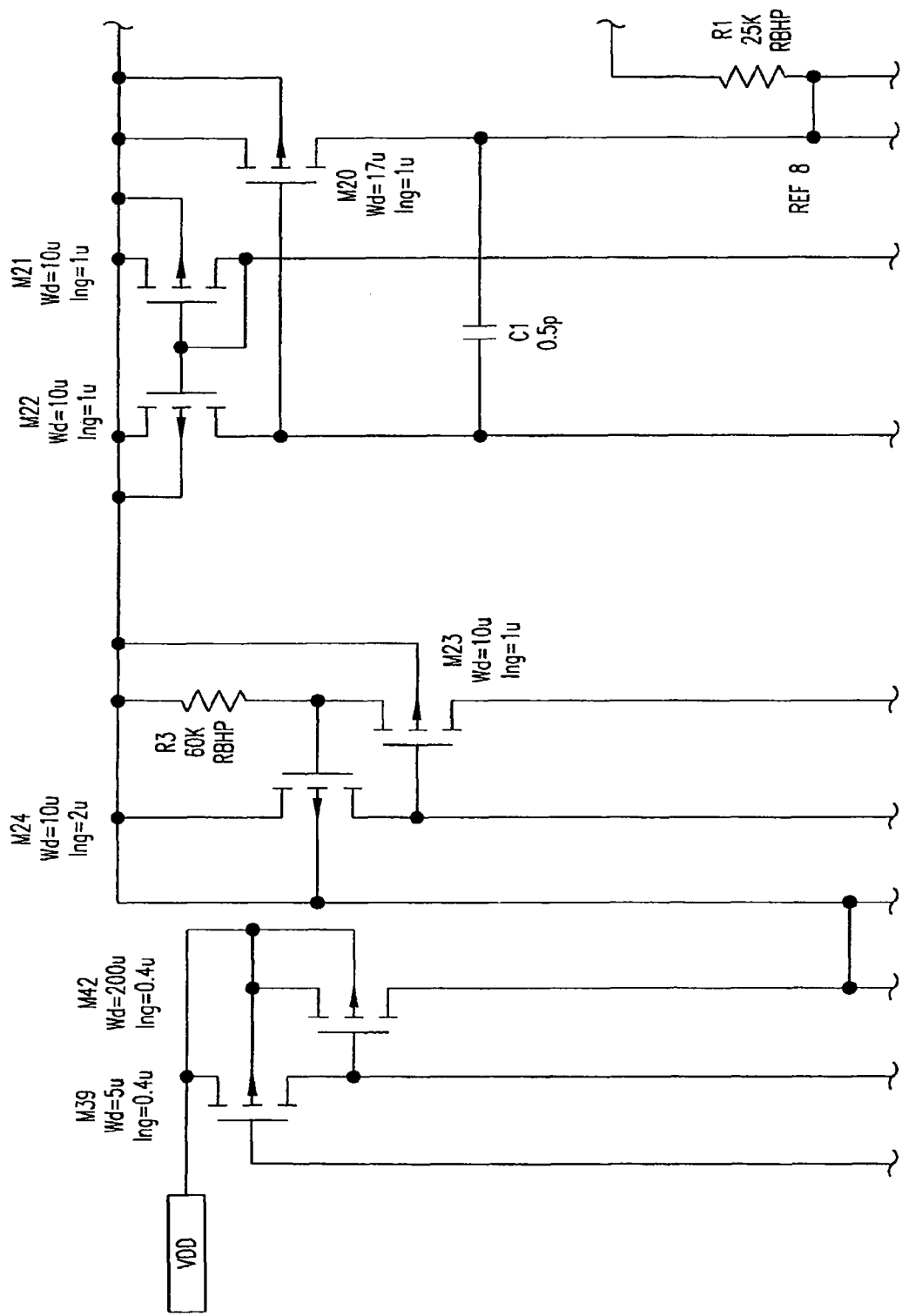


FIG. 123A

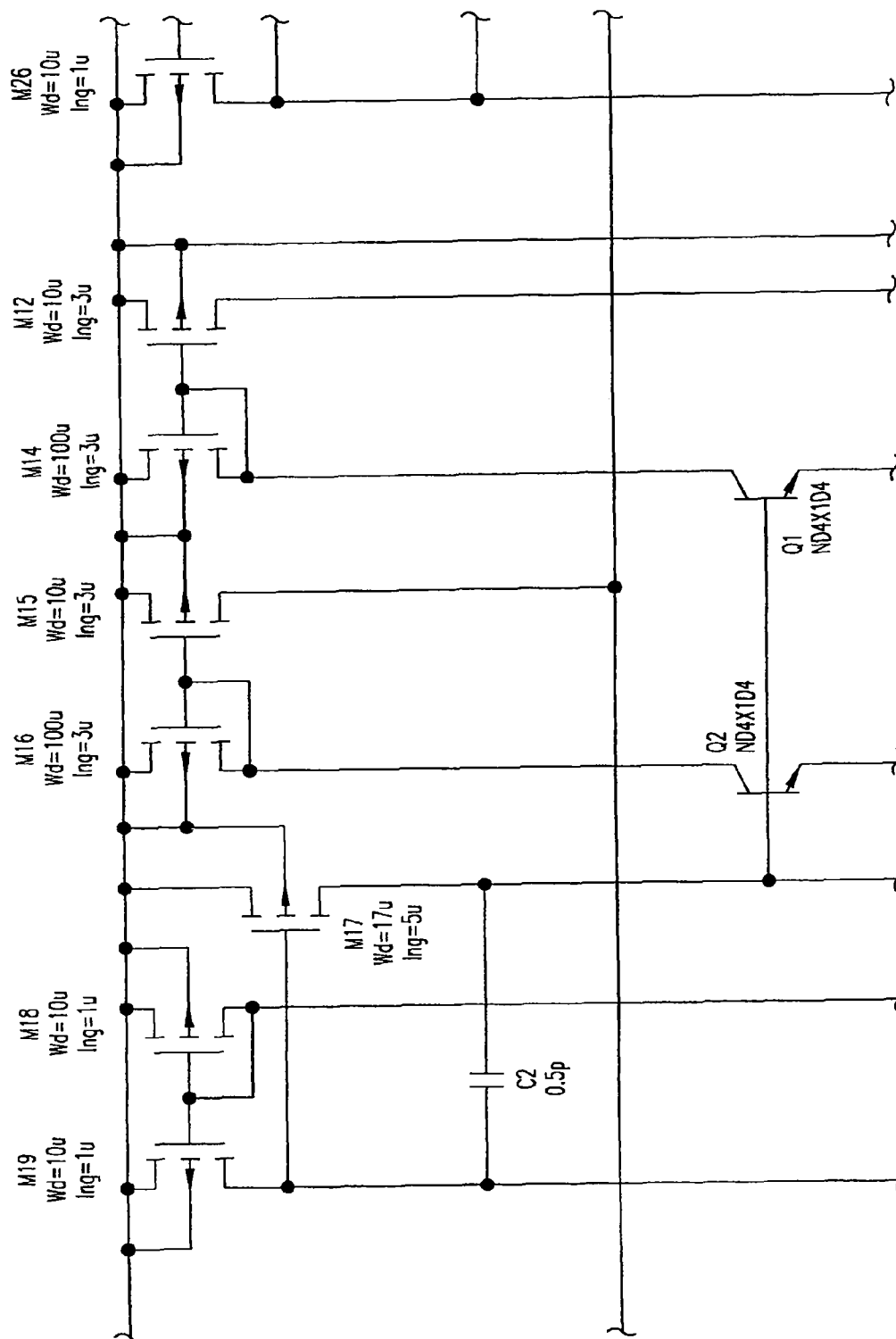


FIG.123B

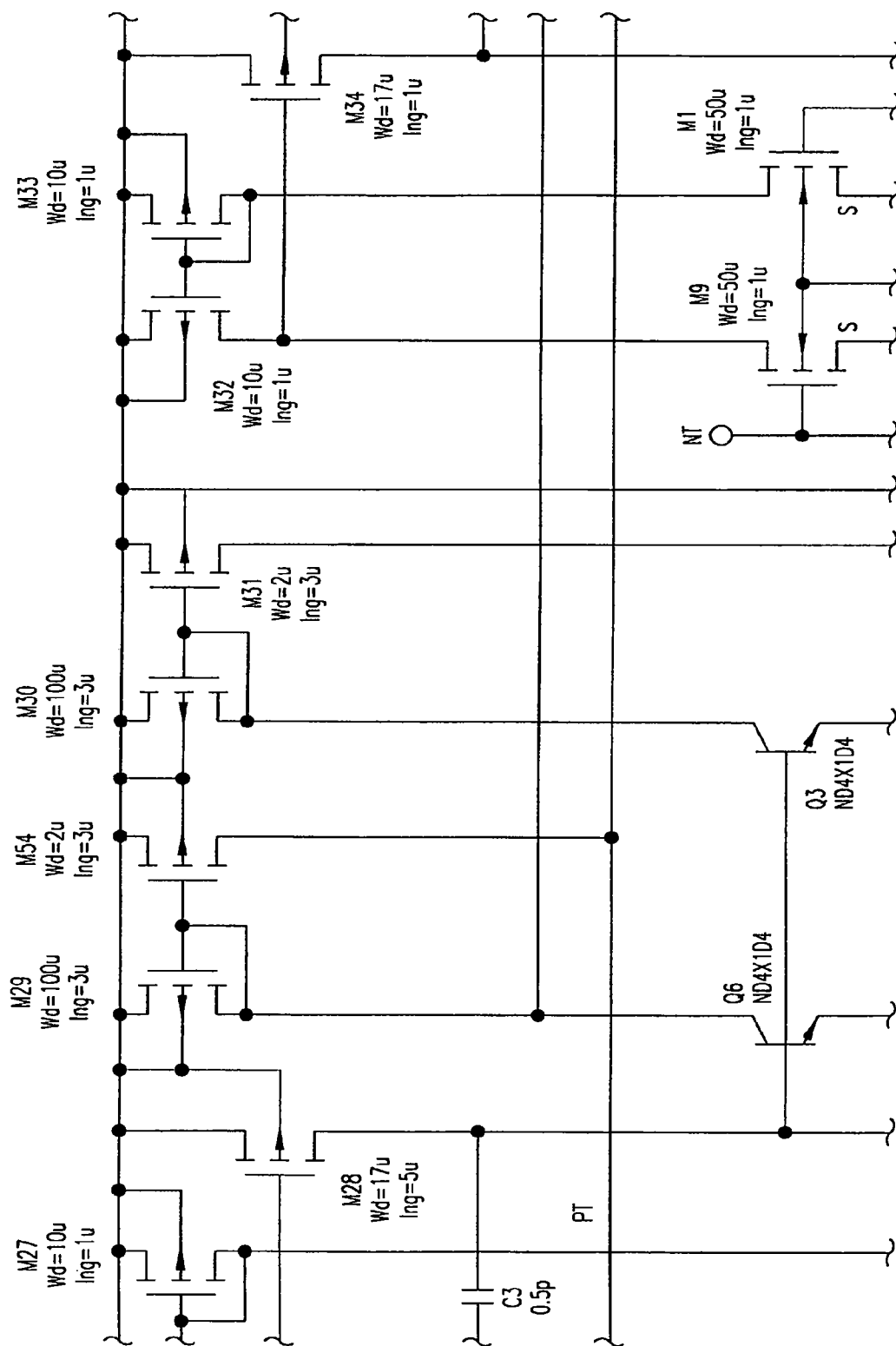


FIG. 123C

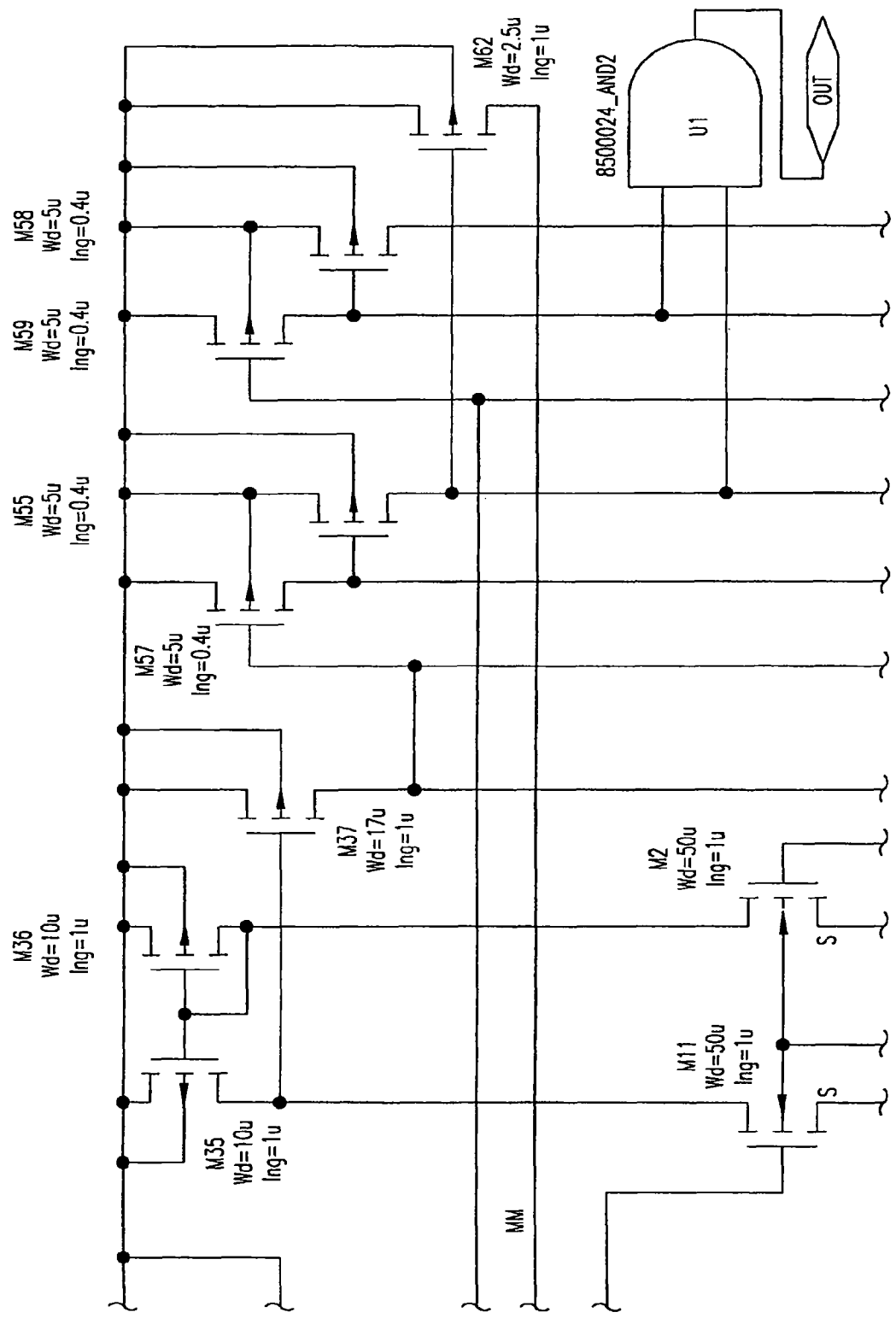
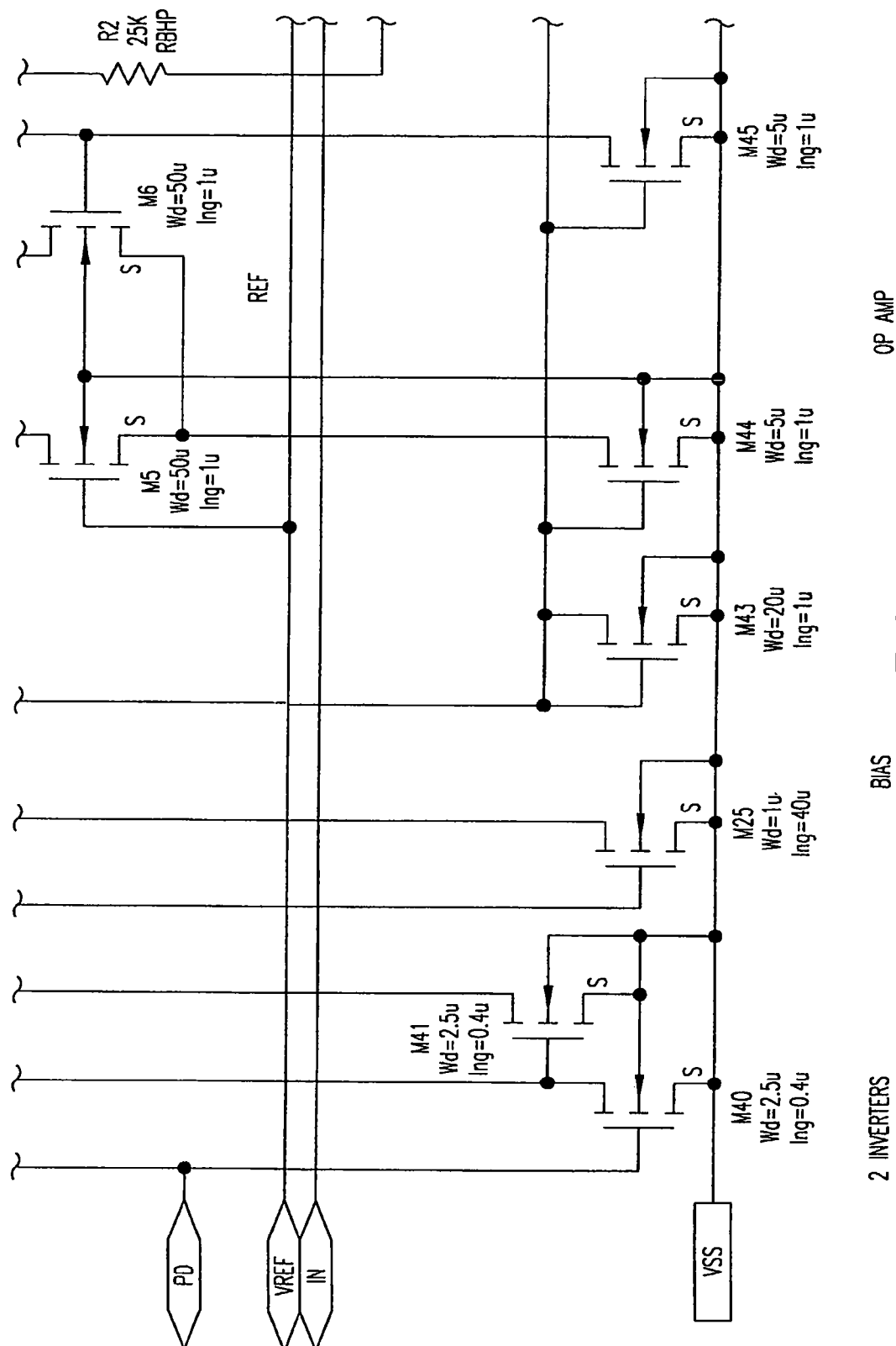
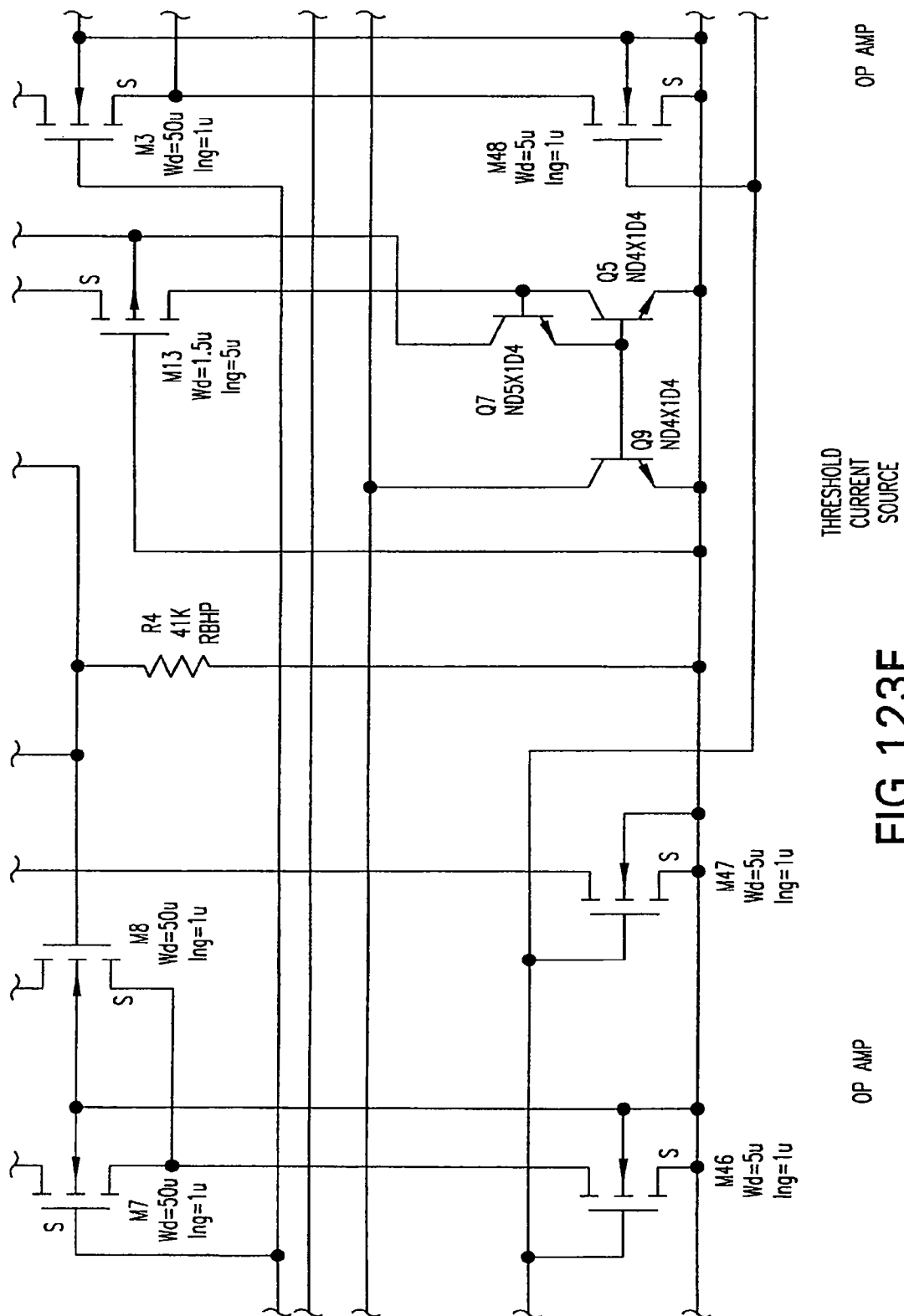


FIG. 123D





**FIG. 123E**



**FIG. 123F**

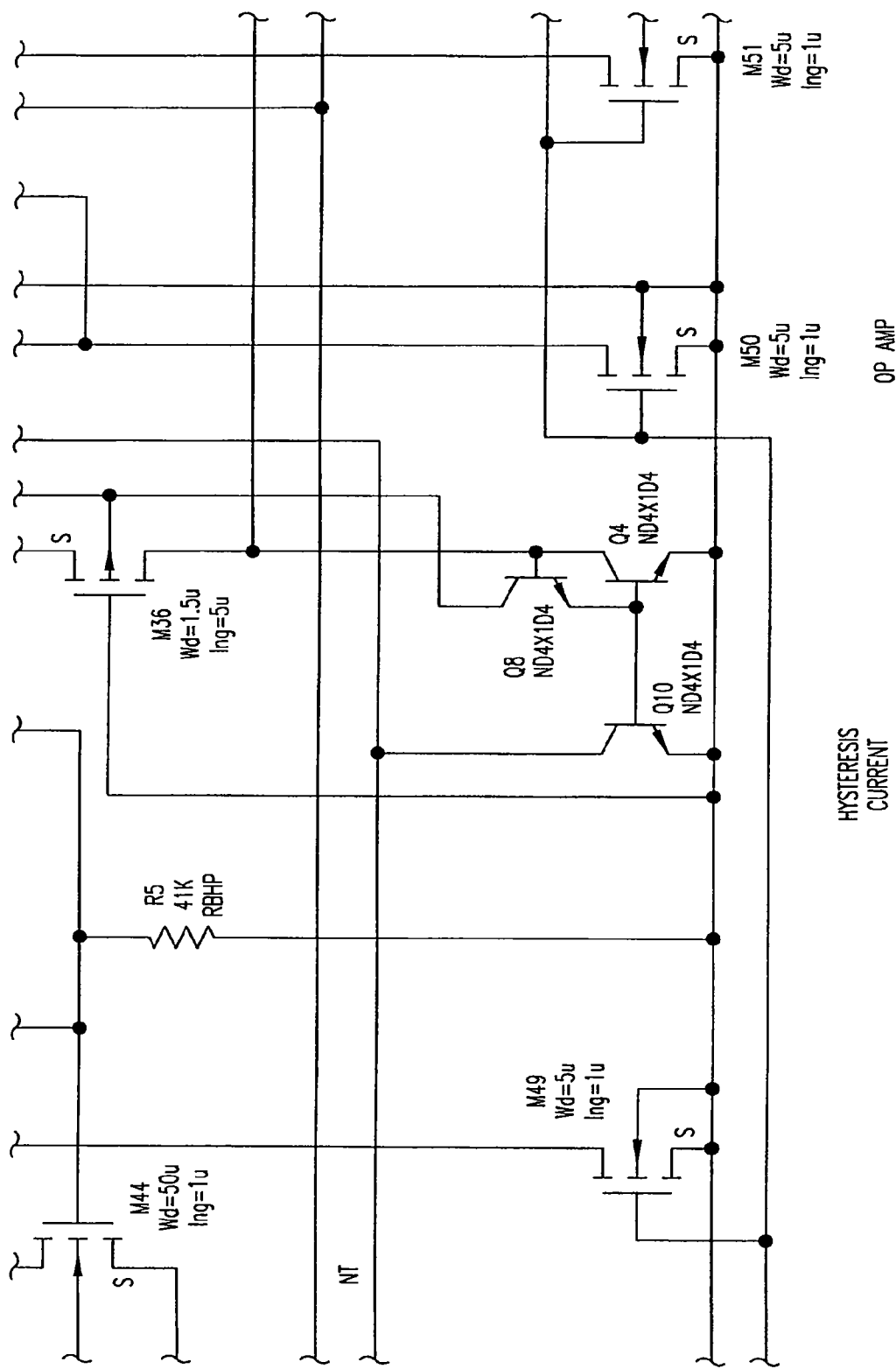
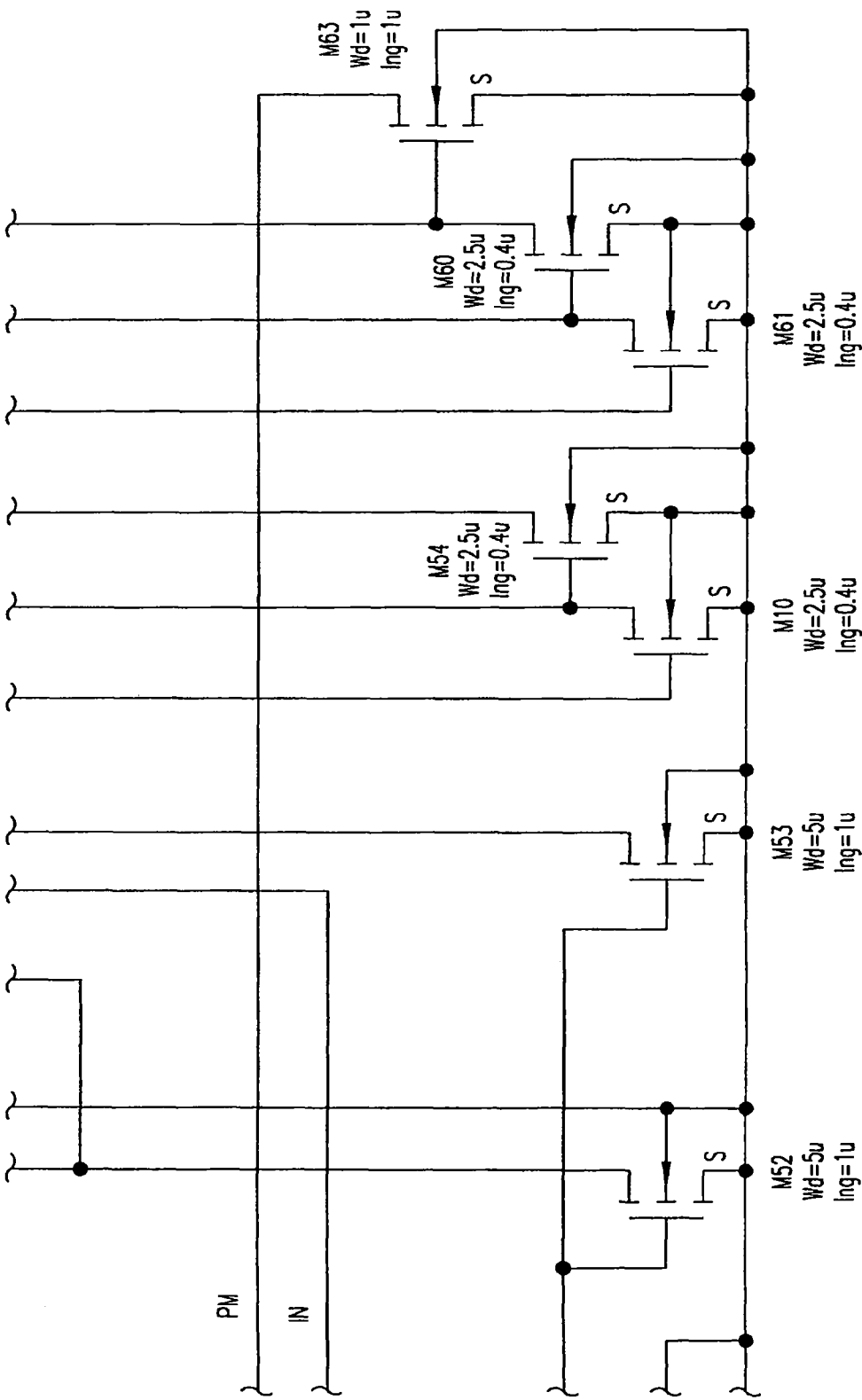


FIG. 123G



4 INVERTERS

OP AMP

FIG. 123H

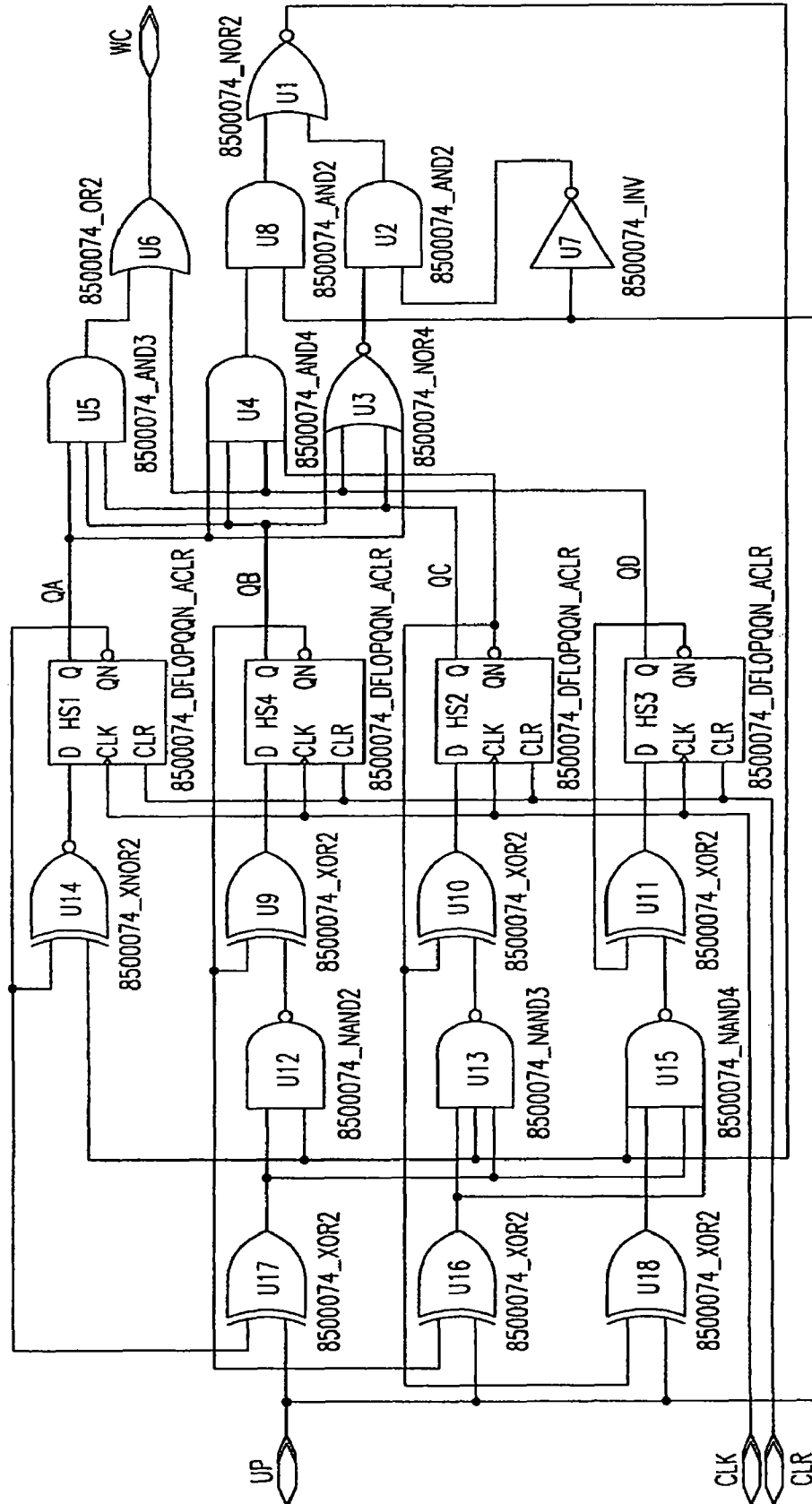


FIG. 124

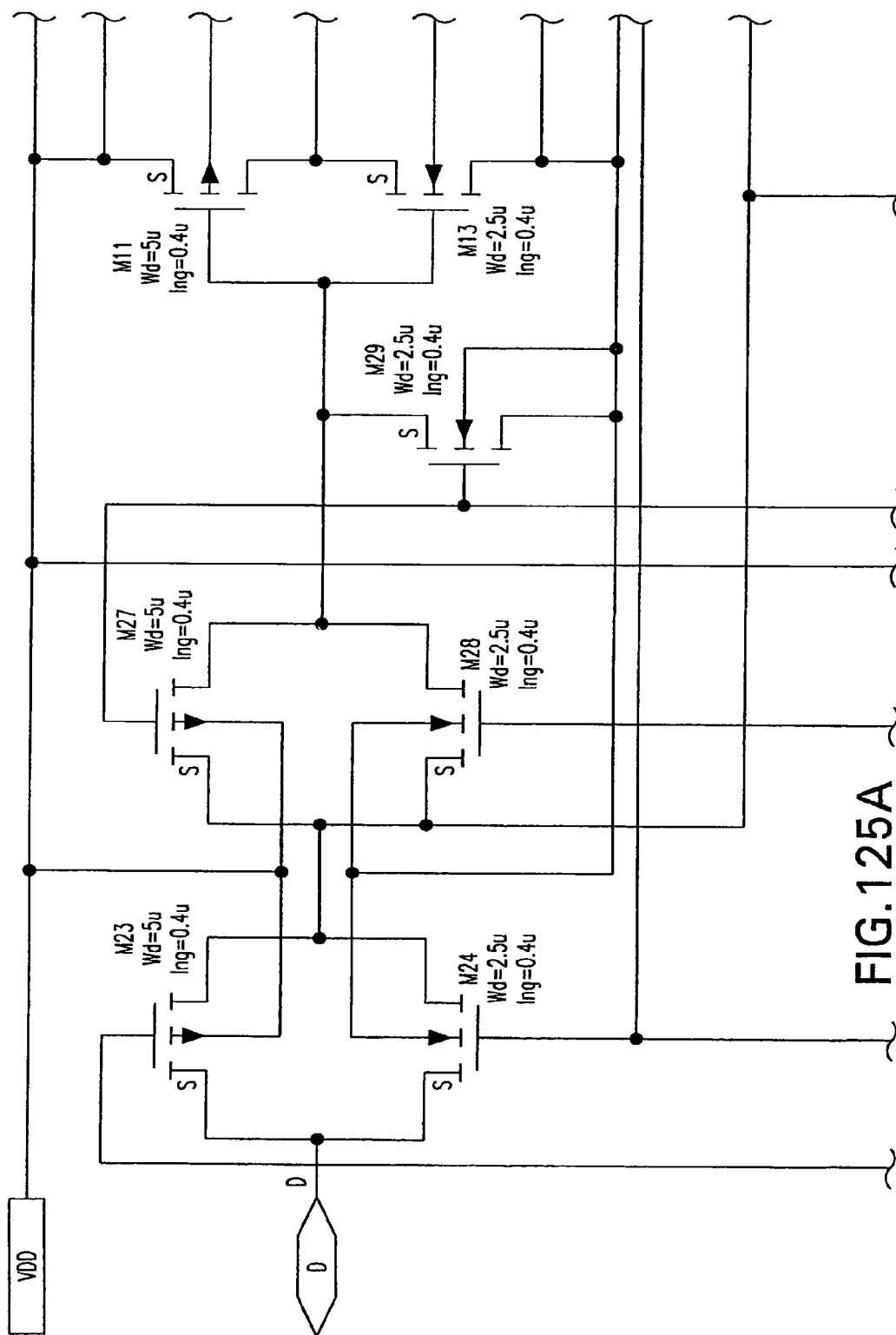
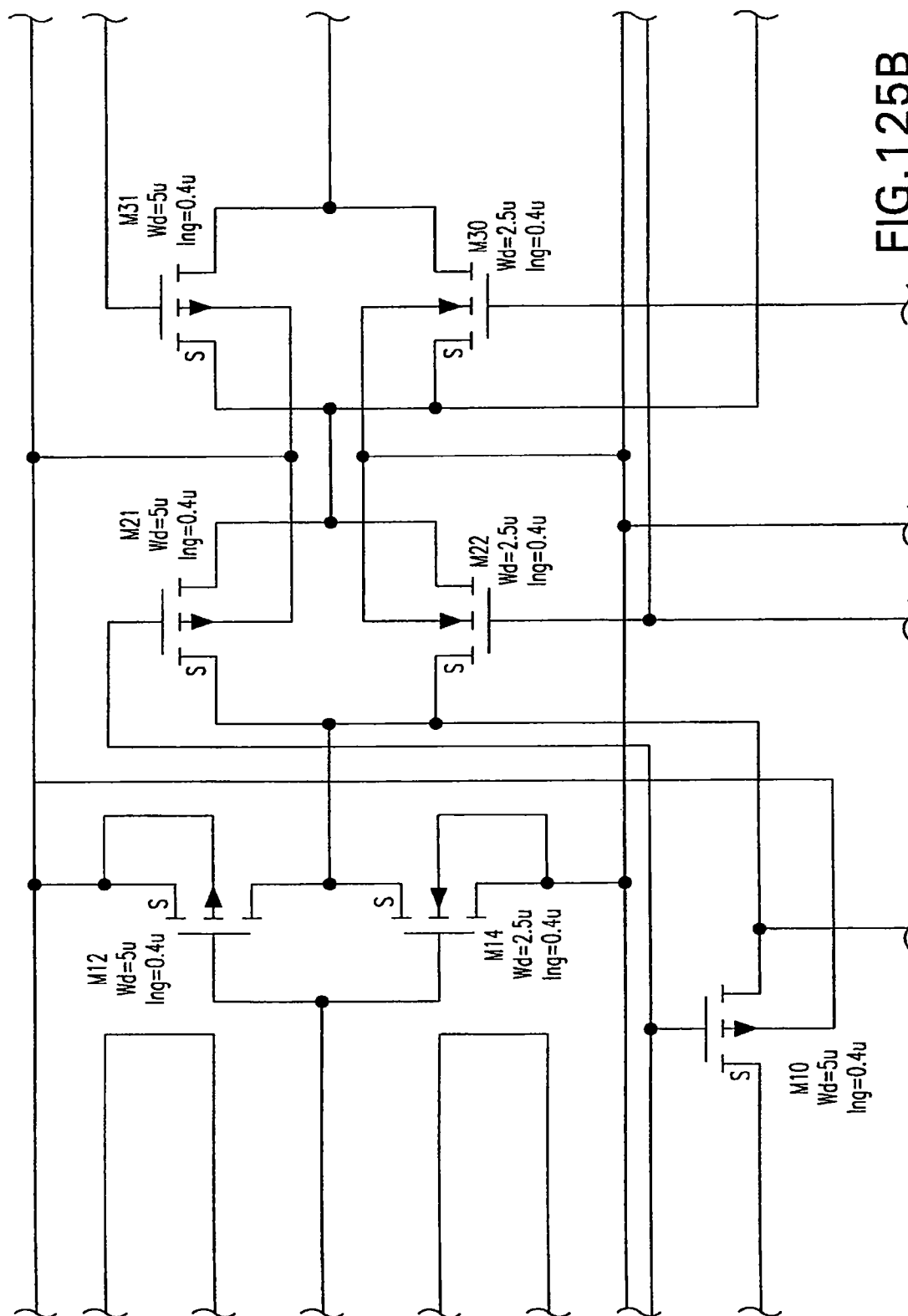


FIG. 125A



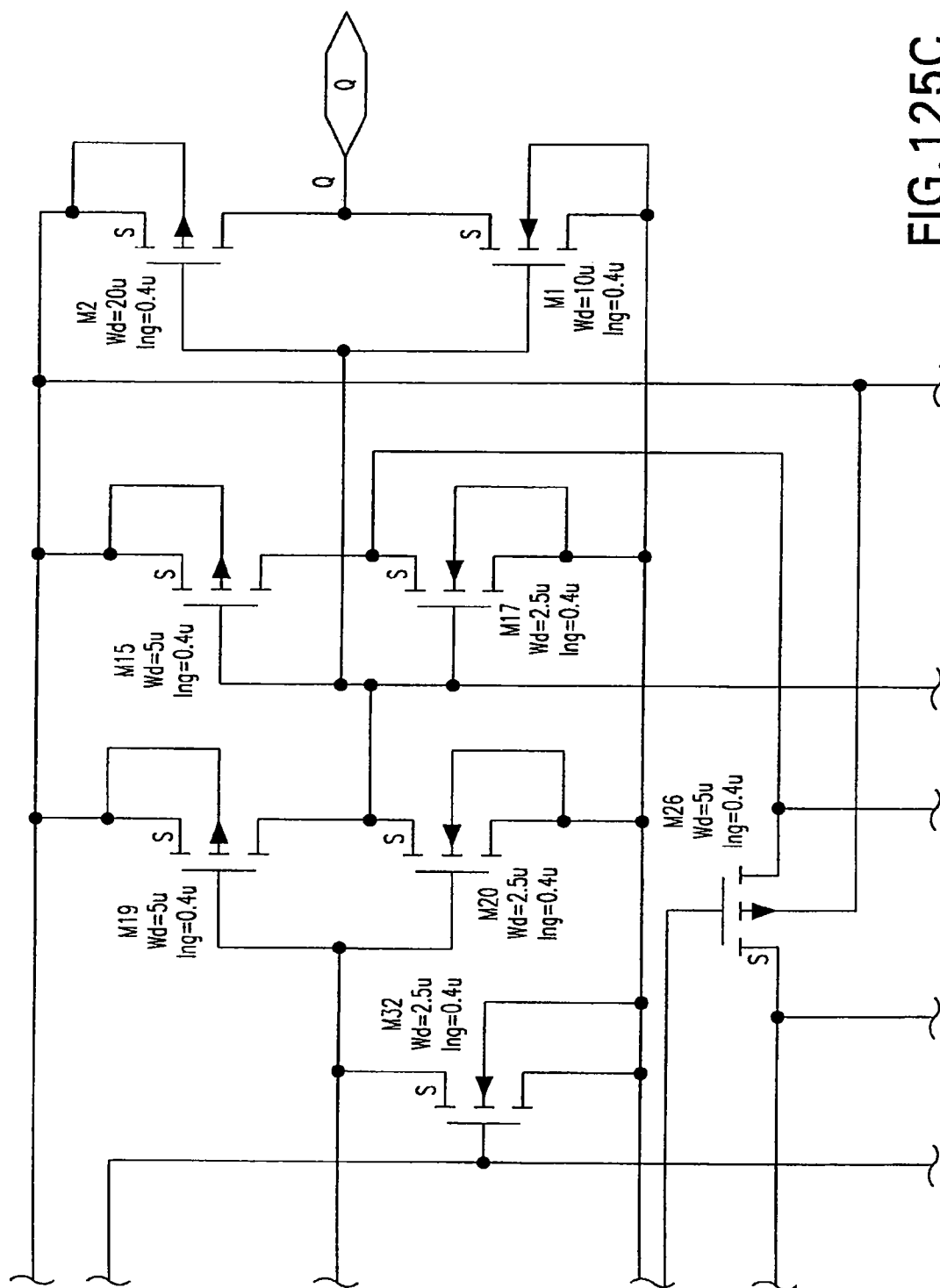
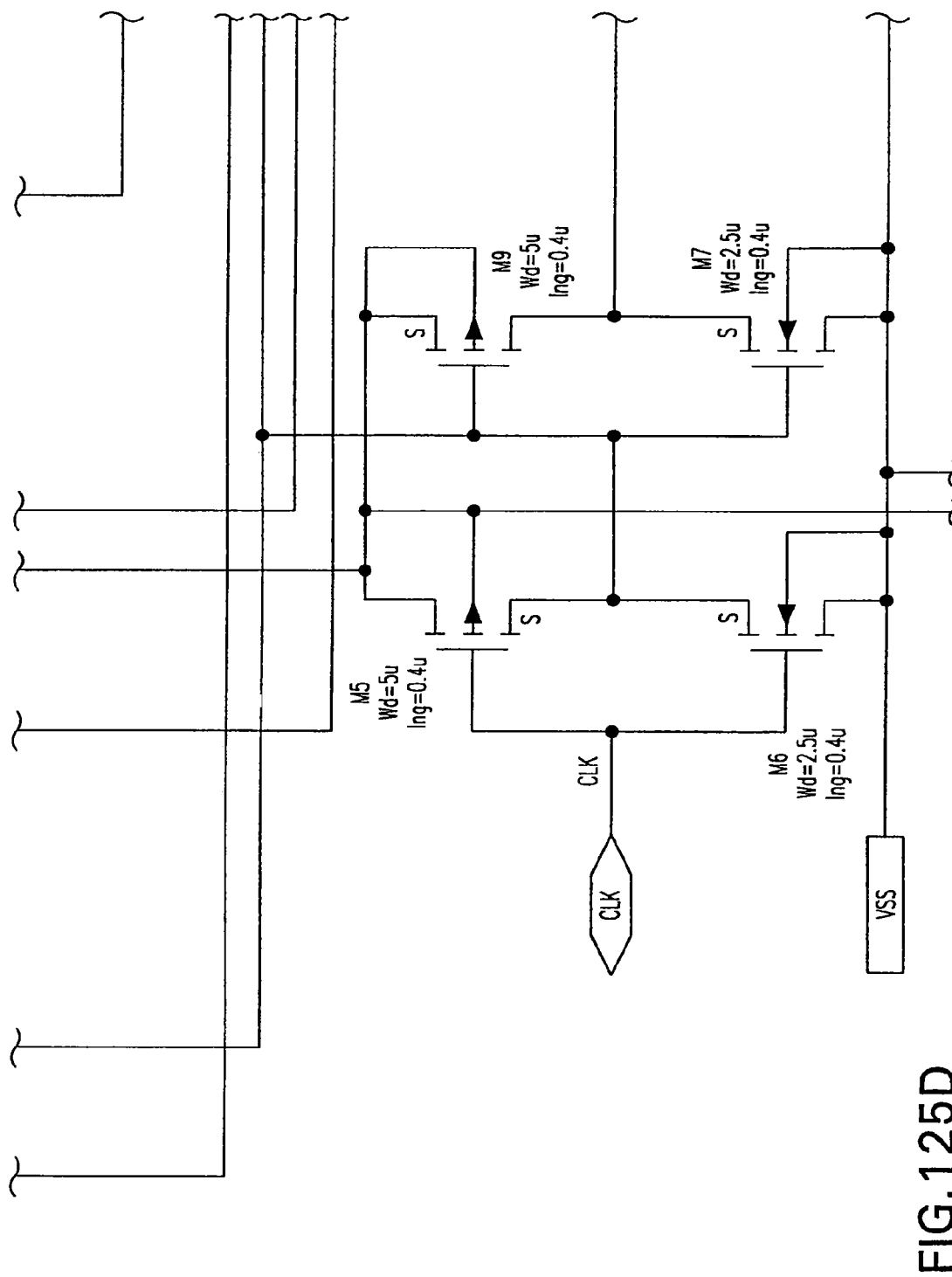


FIG.125C





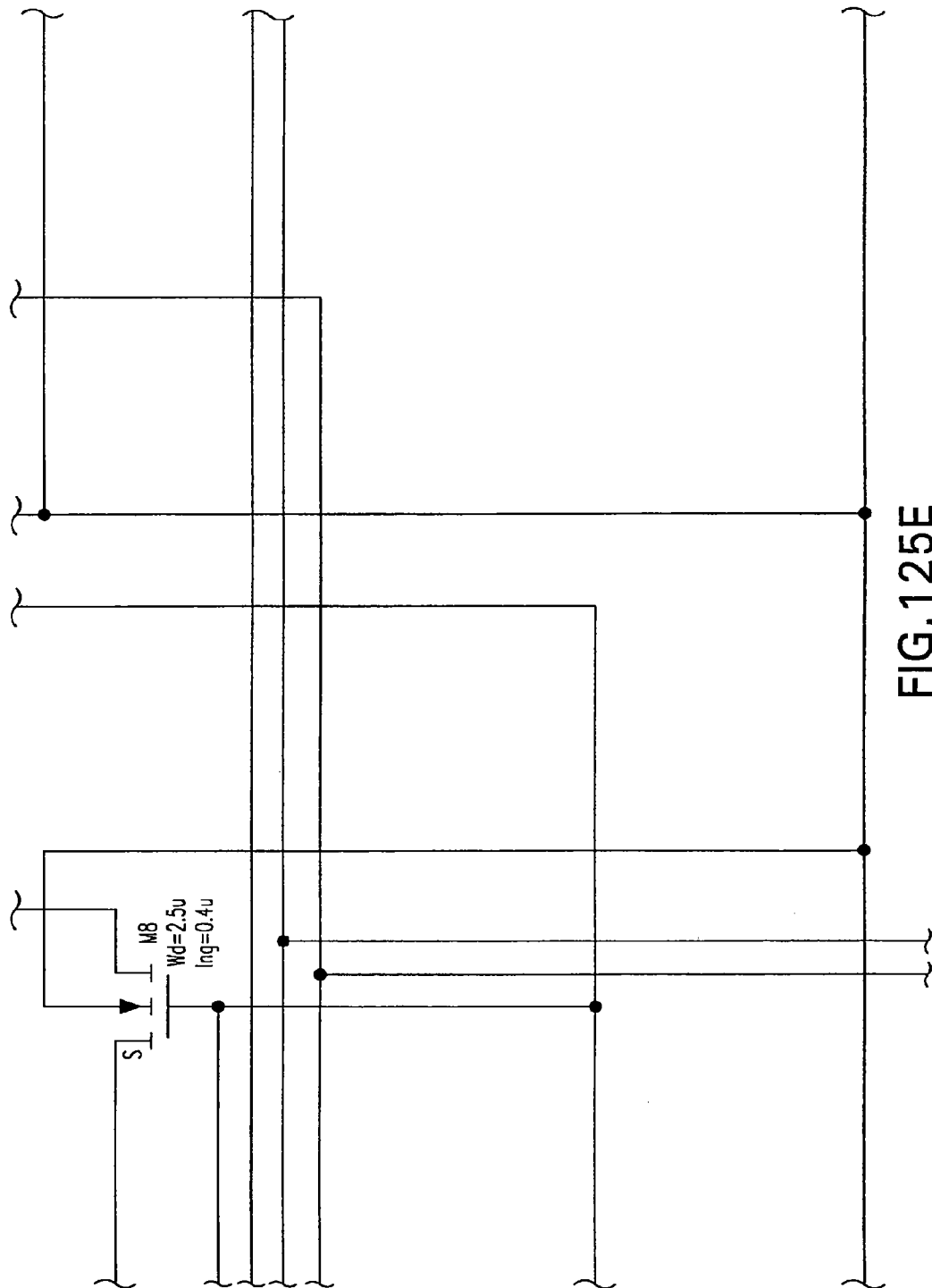


FIG. 125E

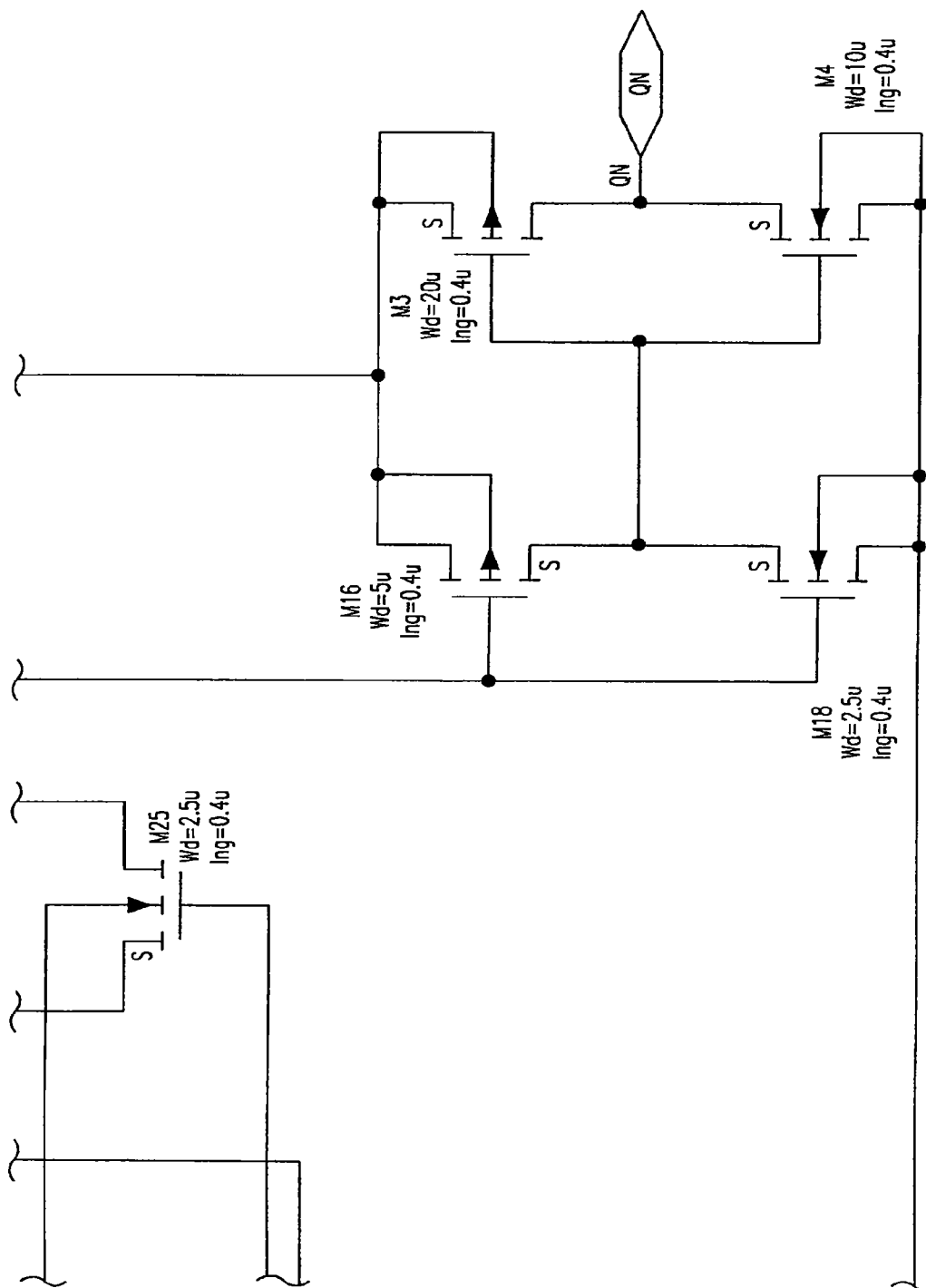


FIG. 125F

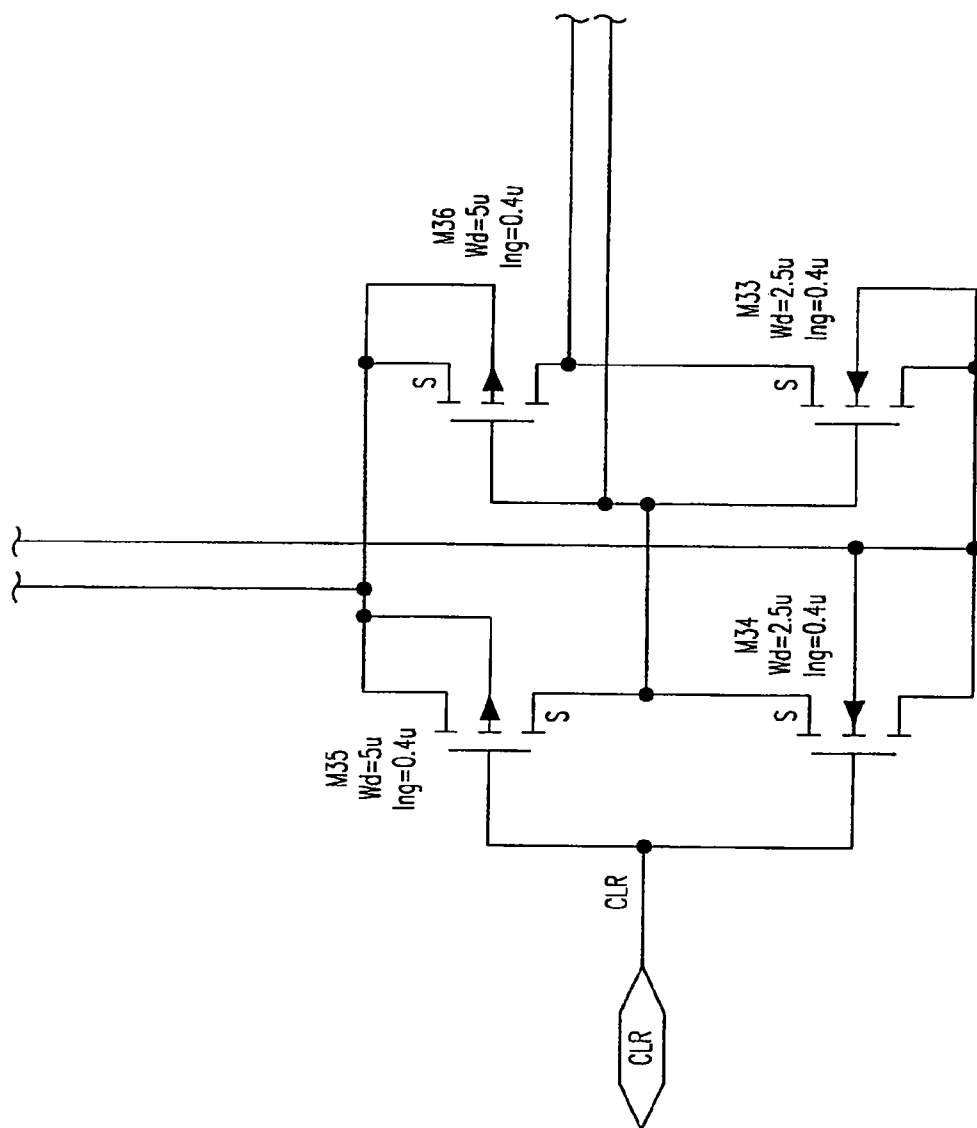


FIG. 125G

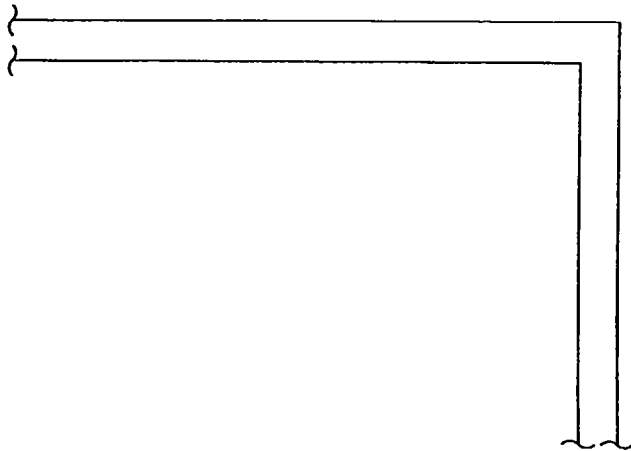


FIG. 125H

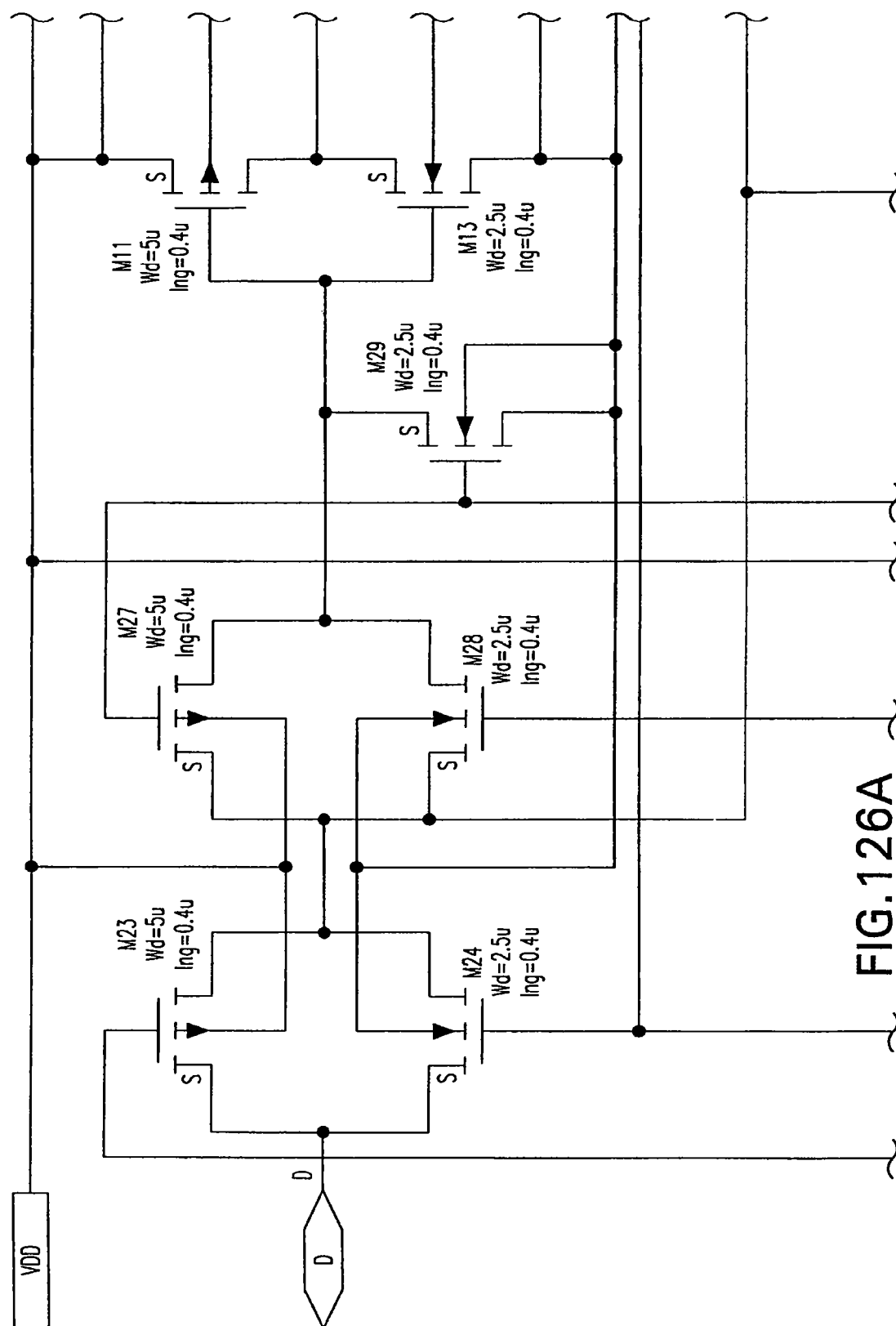


FIG. 126A

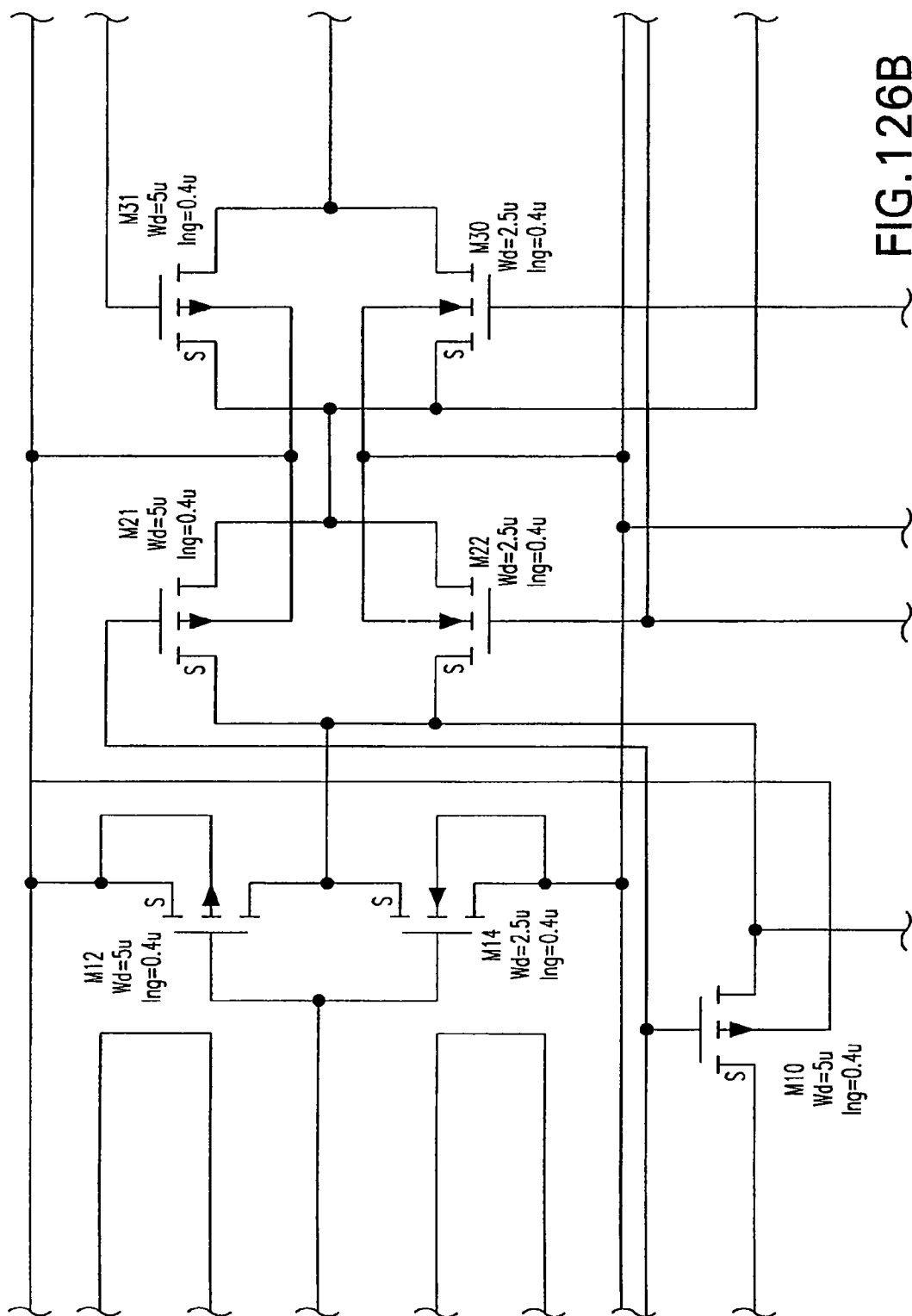
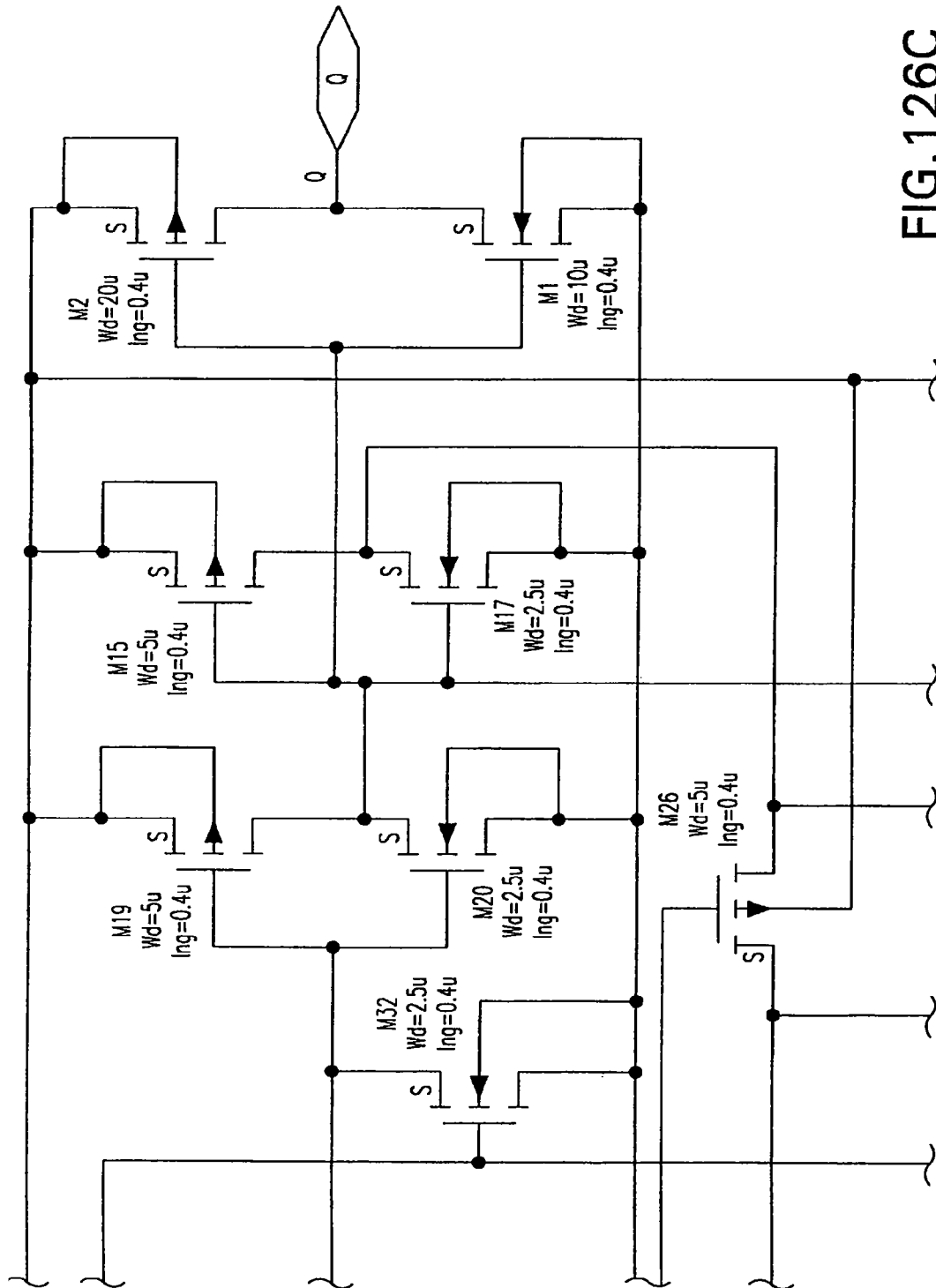
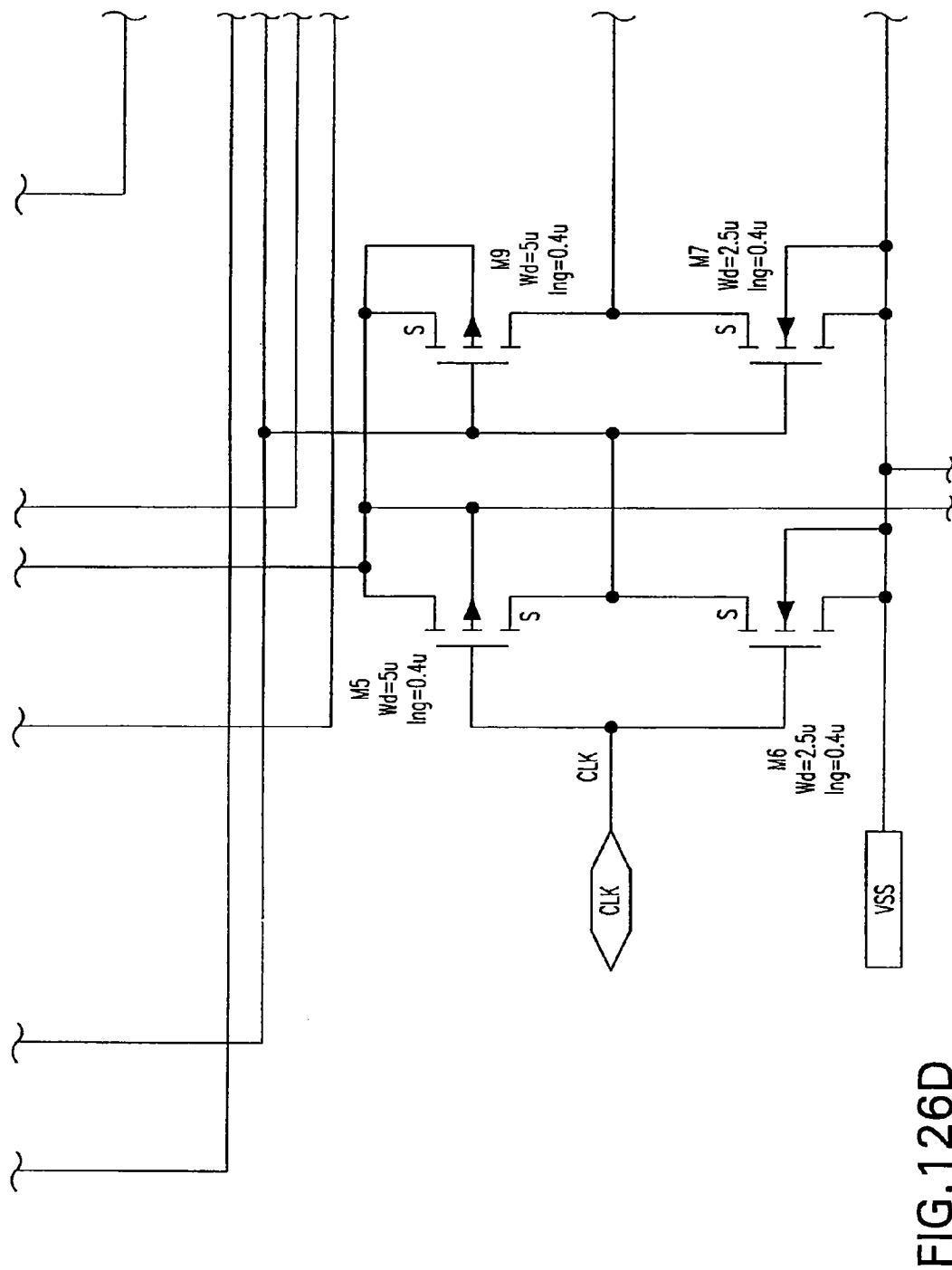
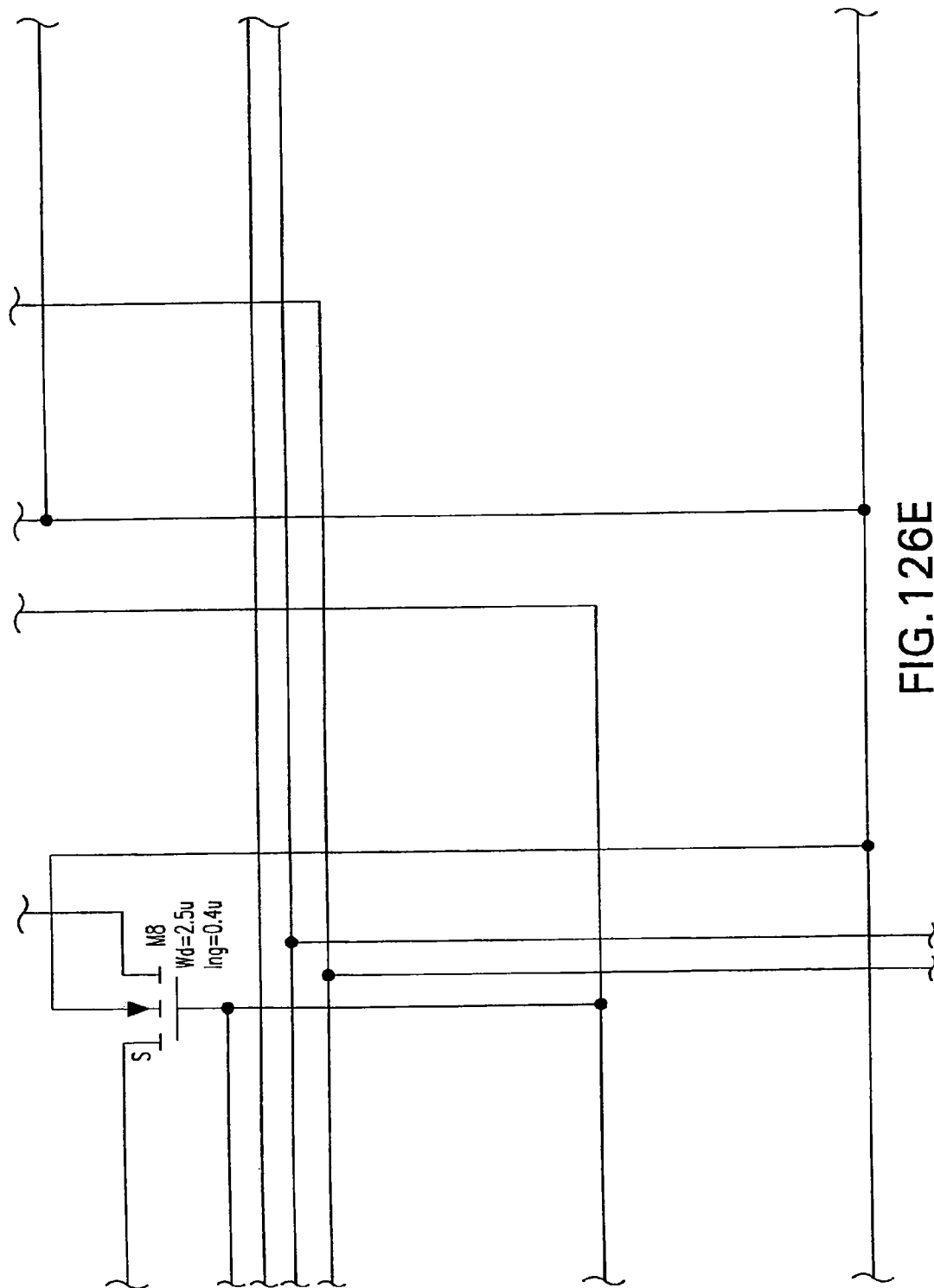


FIG. 126B









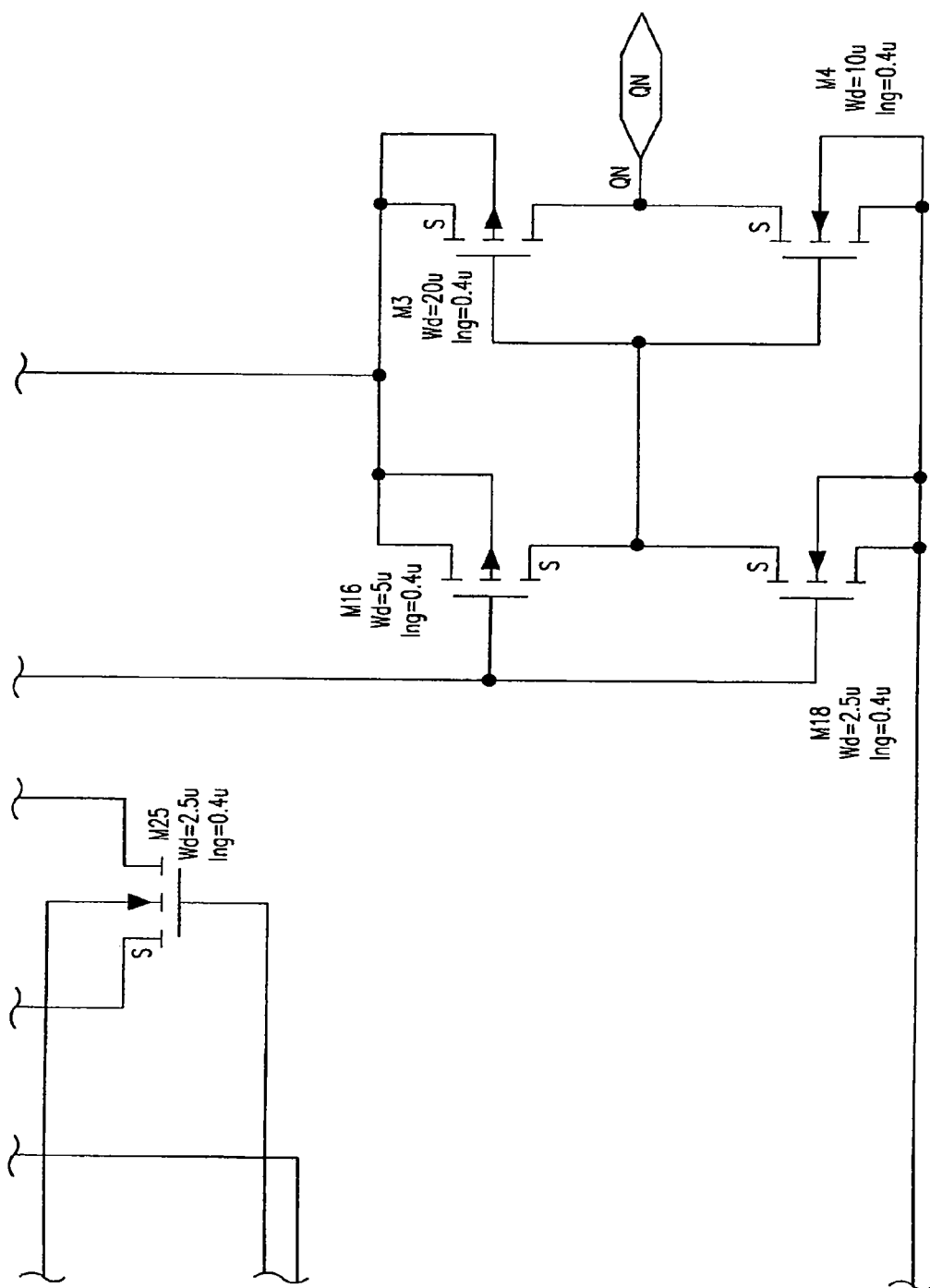


FIG. 126F

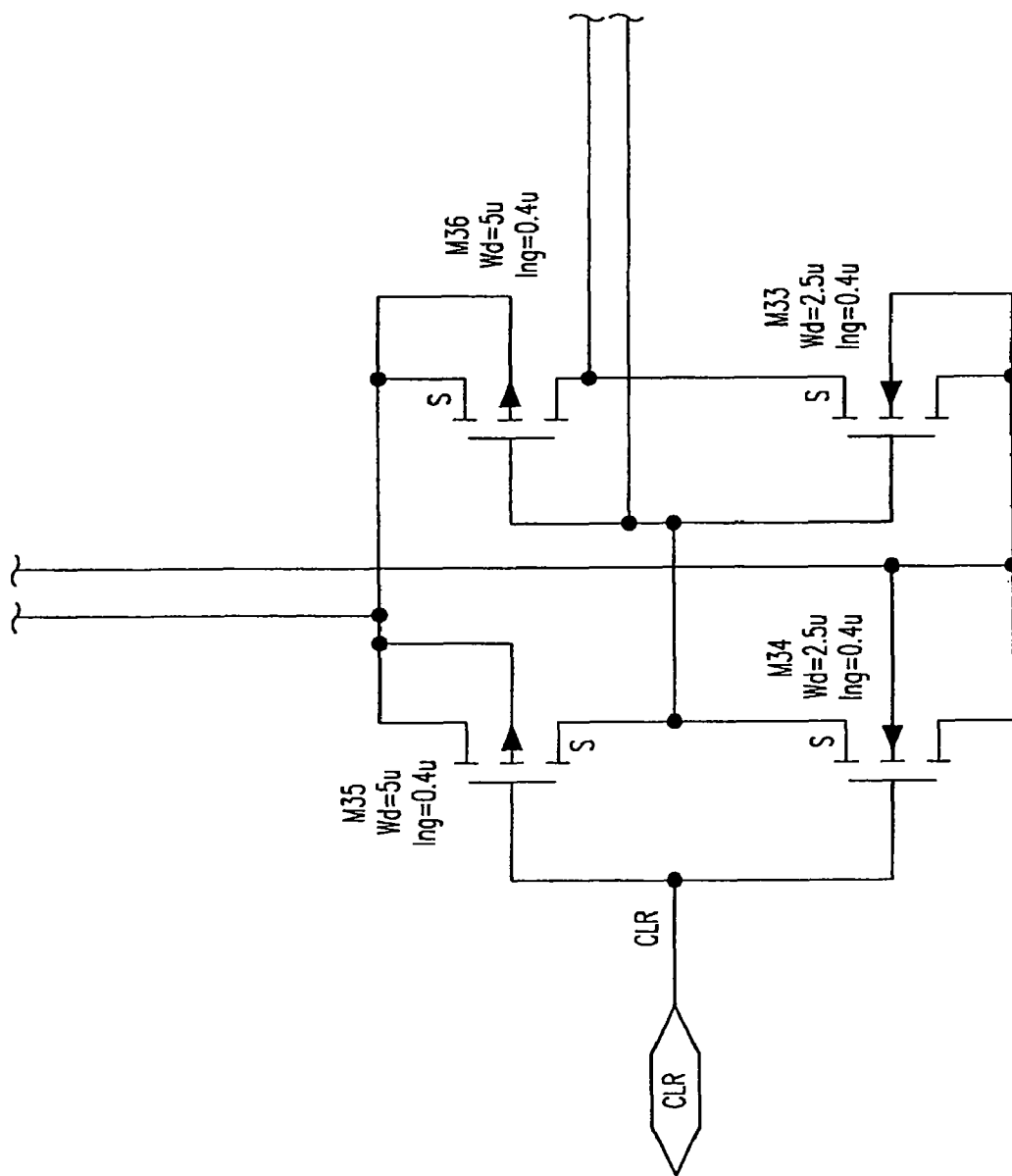
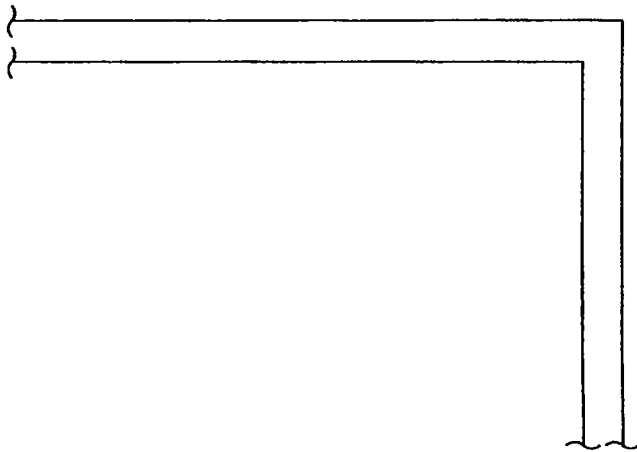


FIG. 126G

FIG. 126H



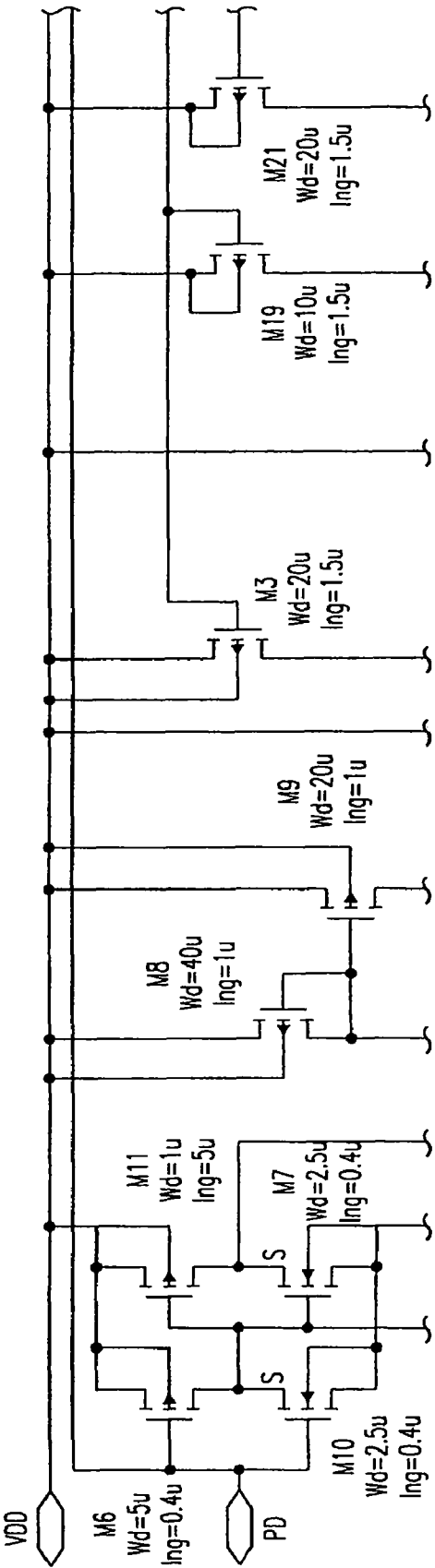


FIG. 127A

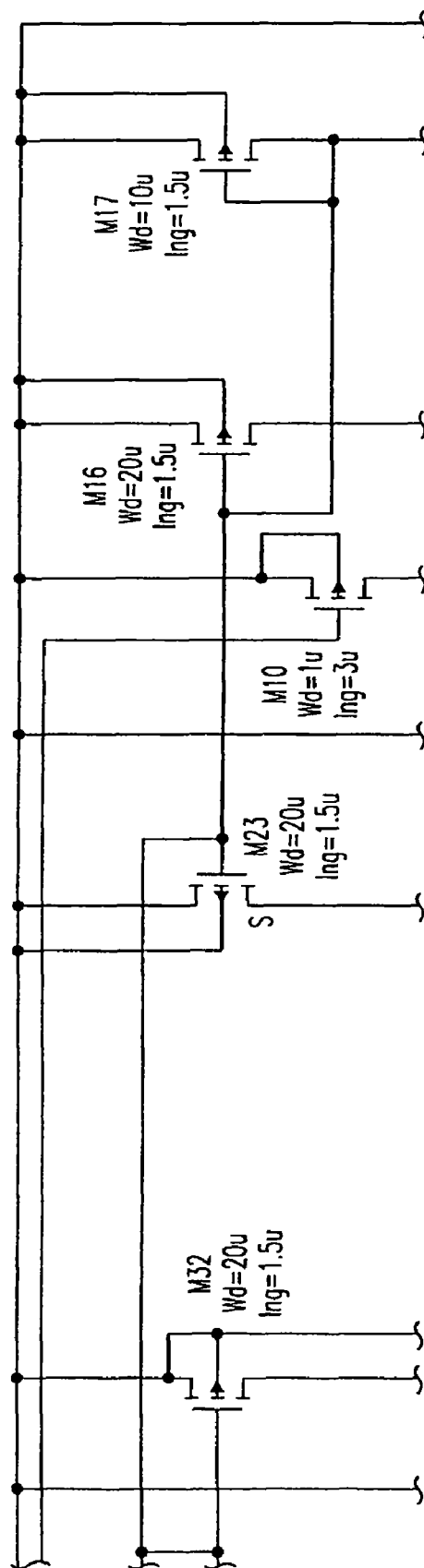
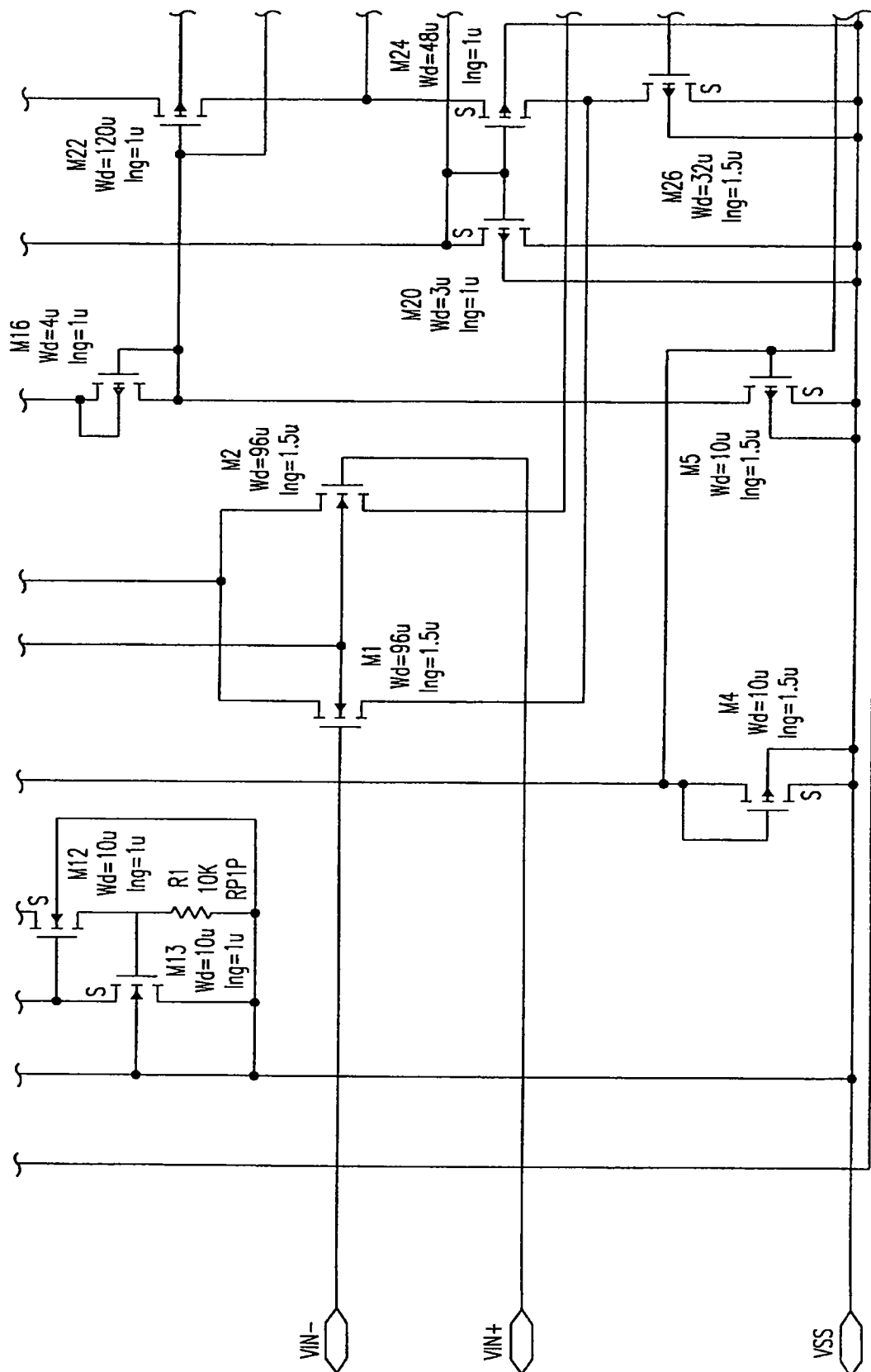


FIG. 127B



**FIG. 127C**



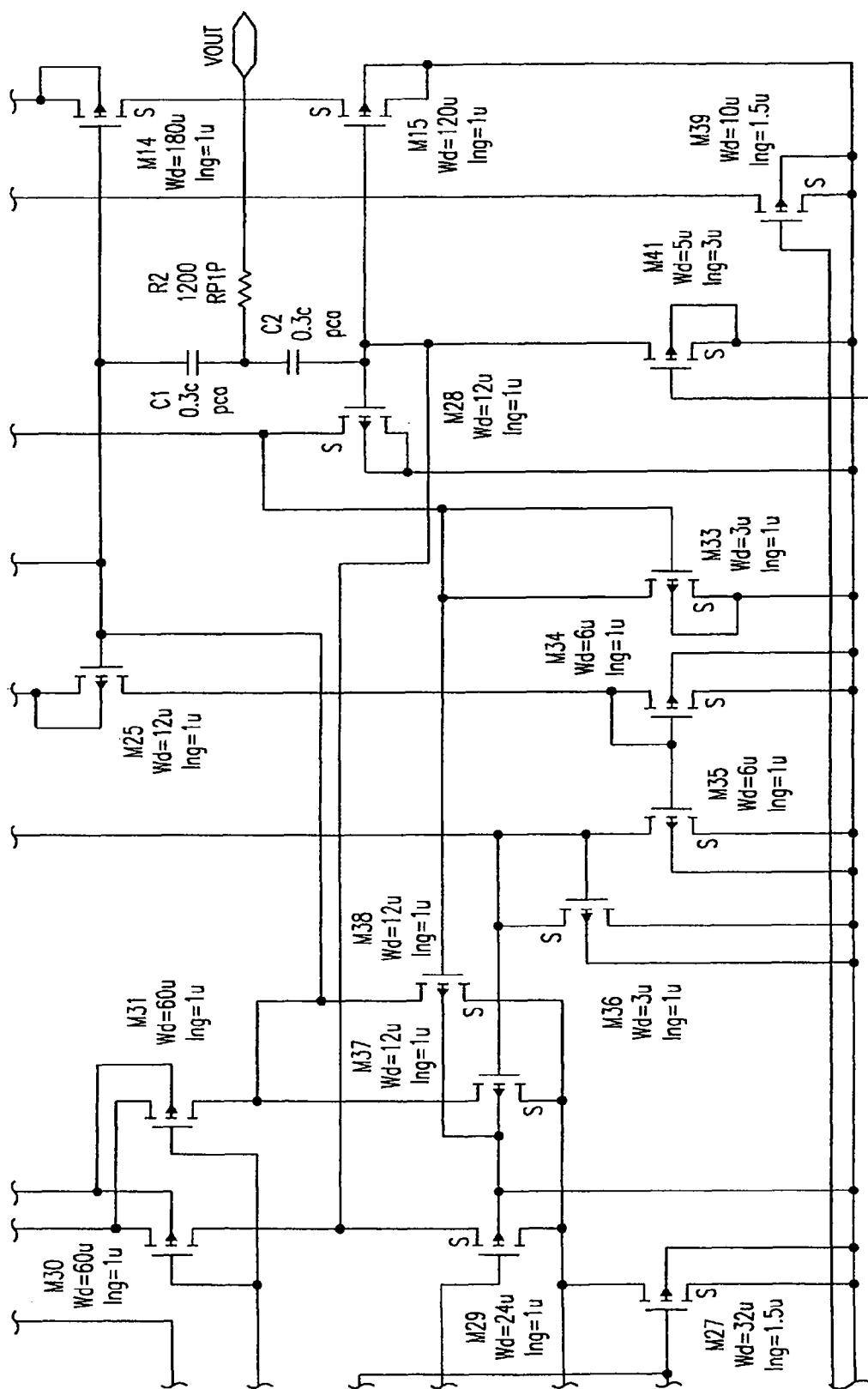


FIG.127D

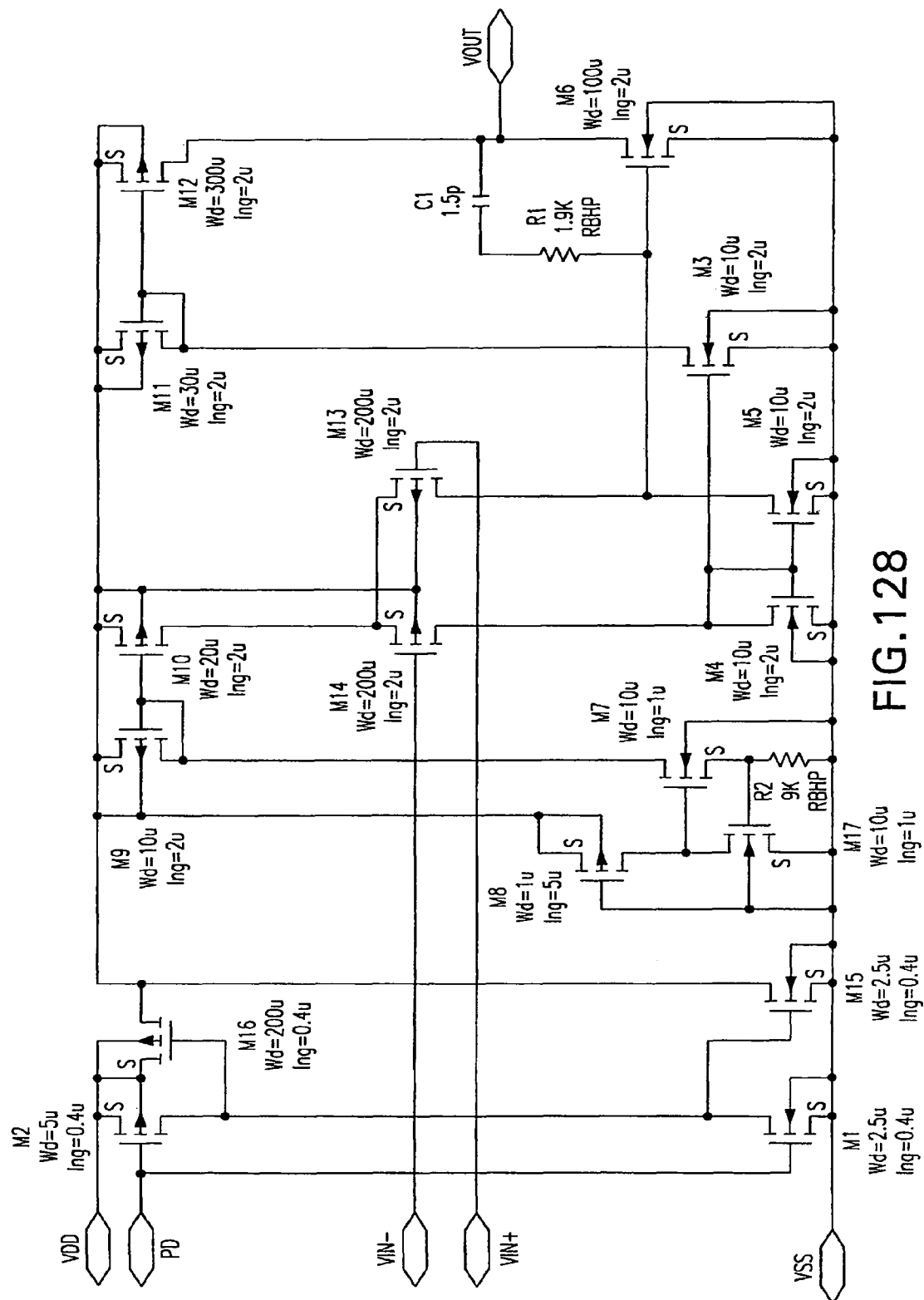


FIG. 128

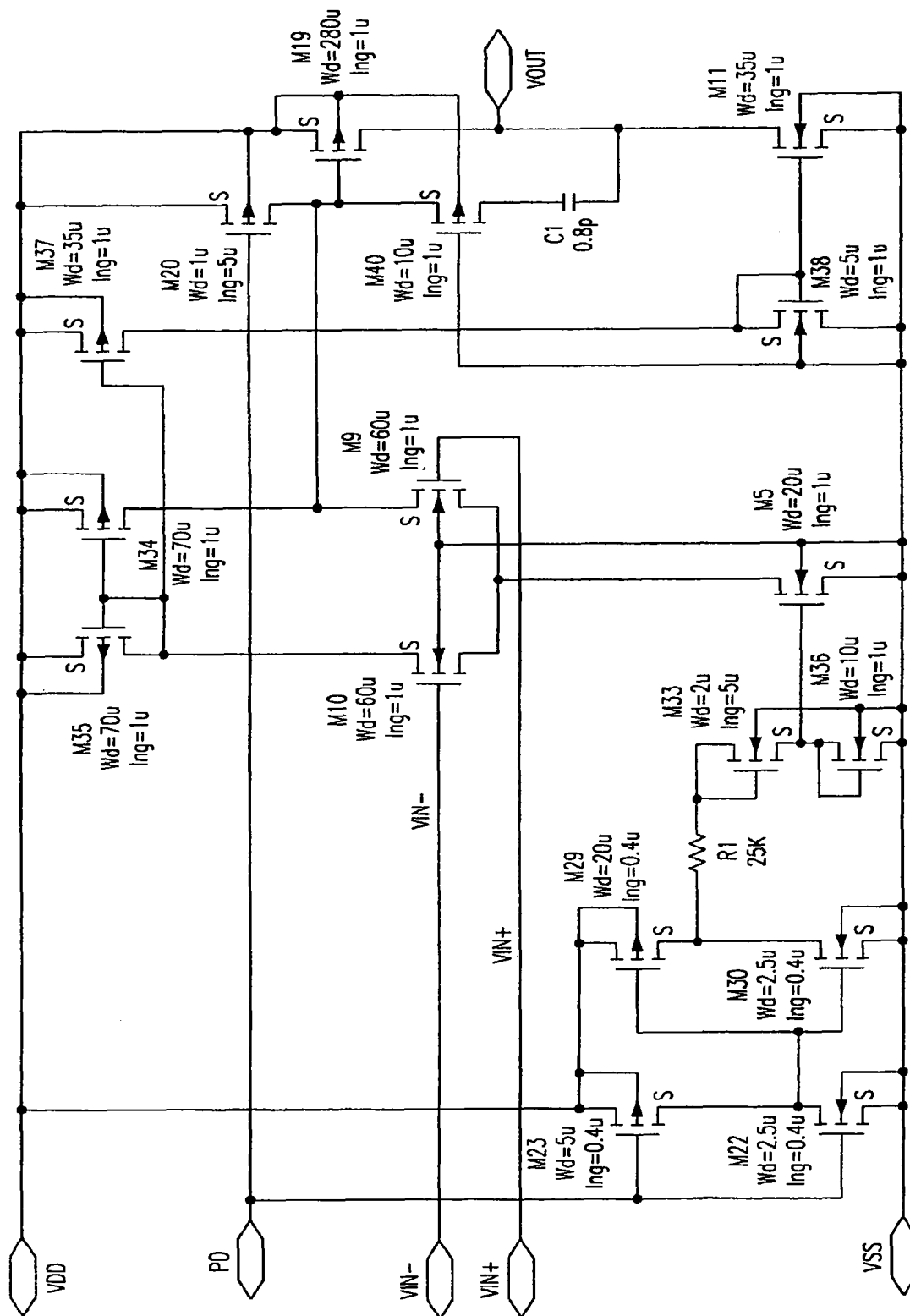


FIG. 129

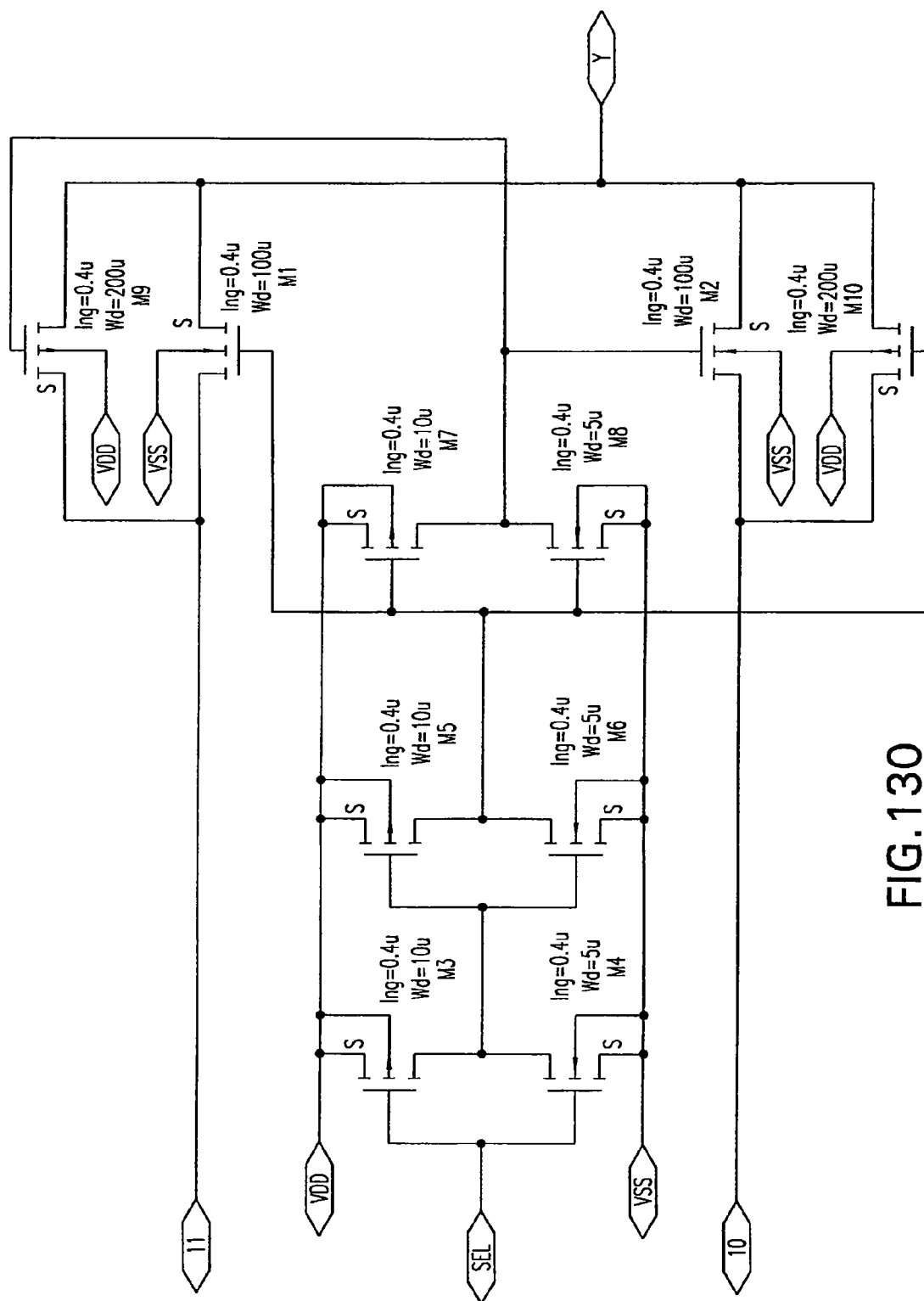


FIG. 130

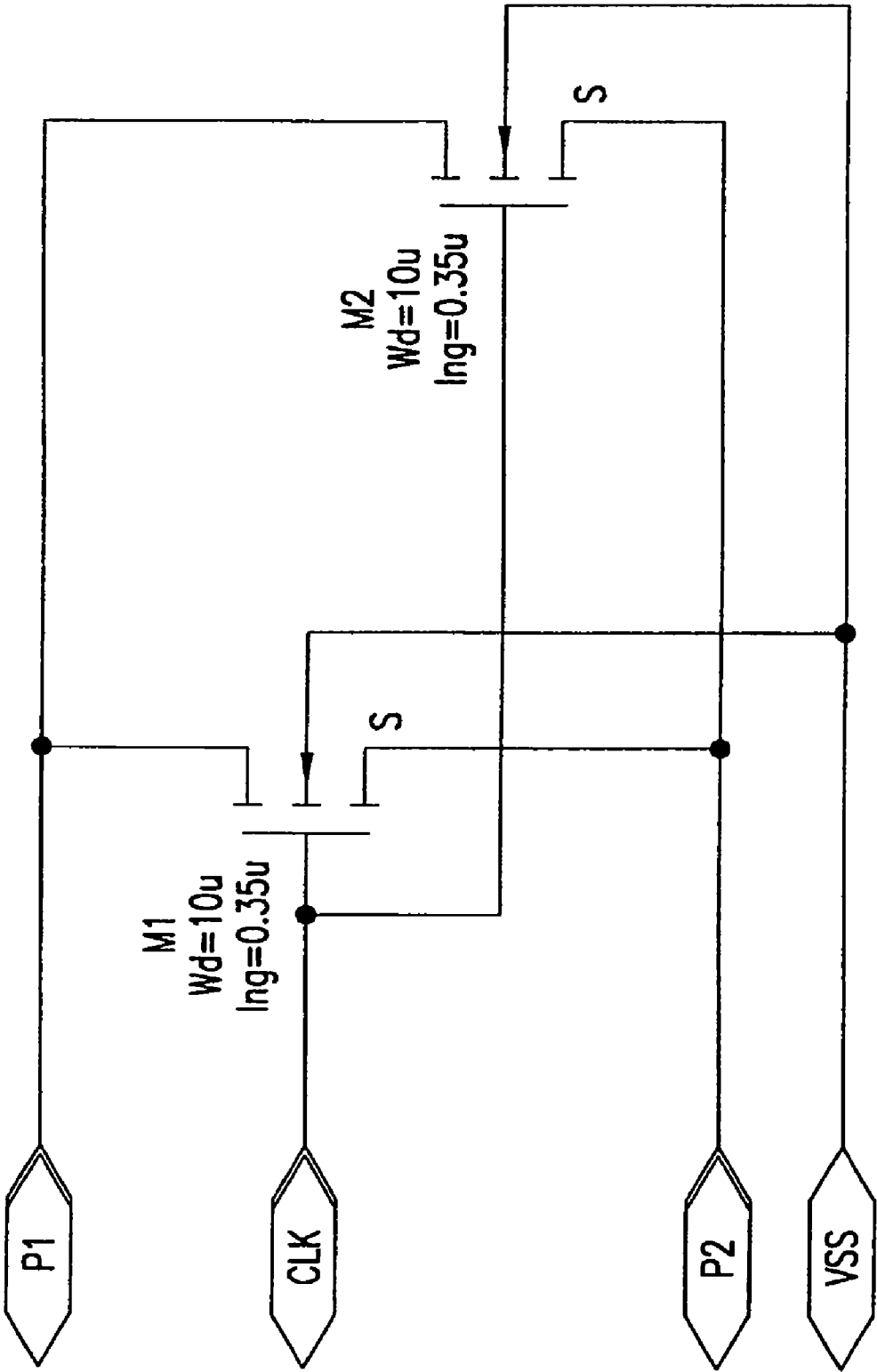


FIG. 131

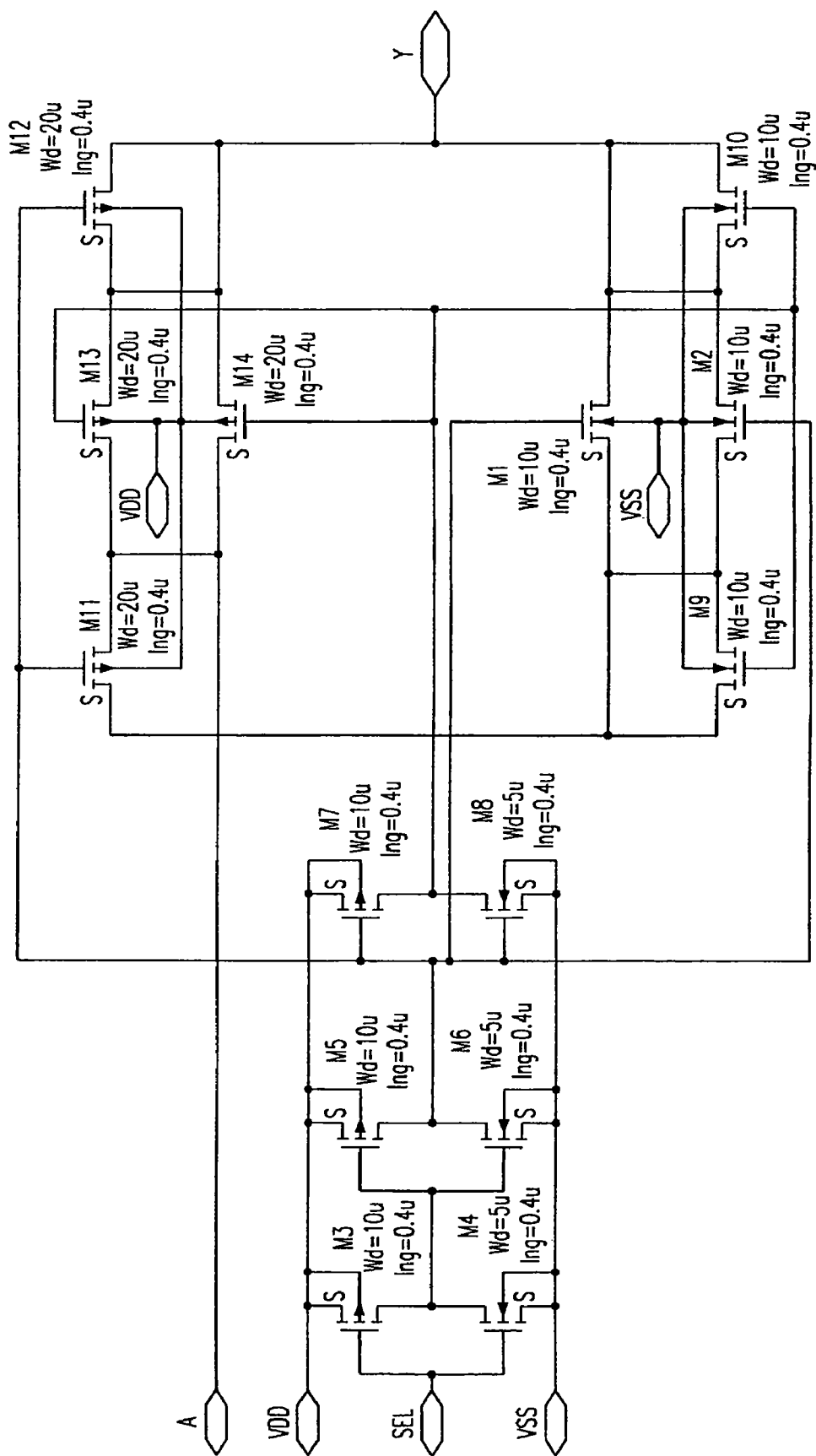
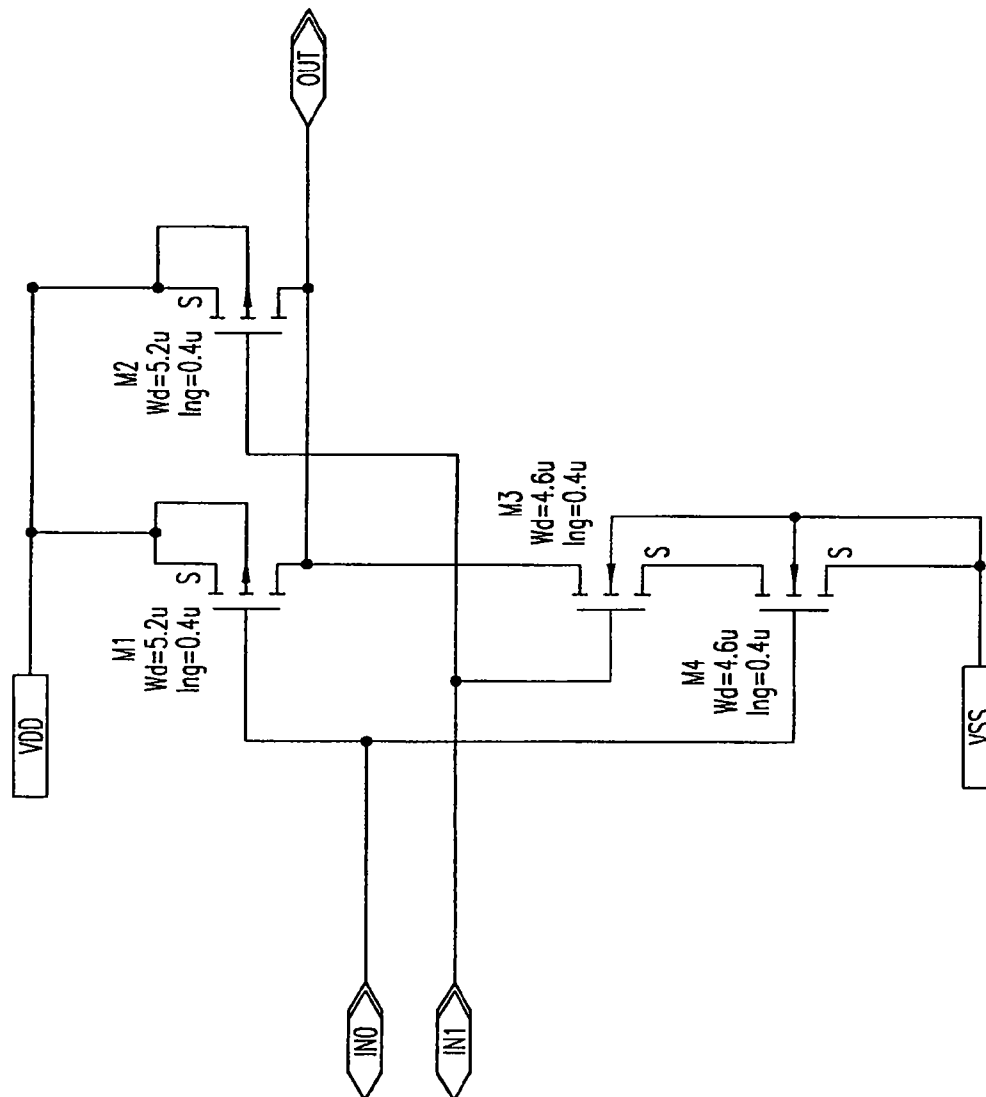
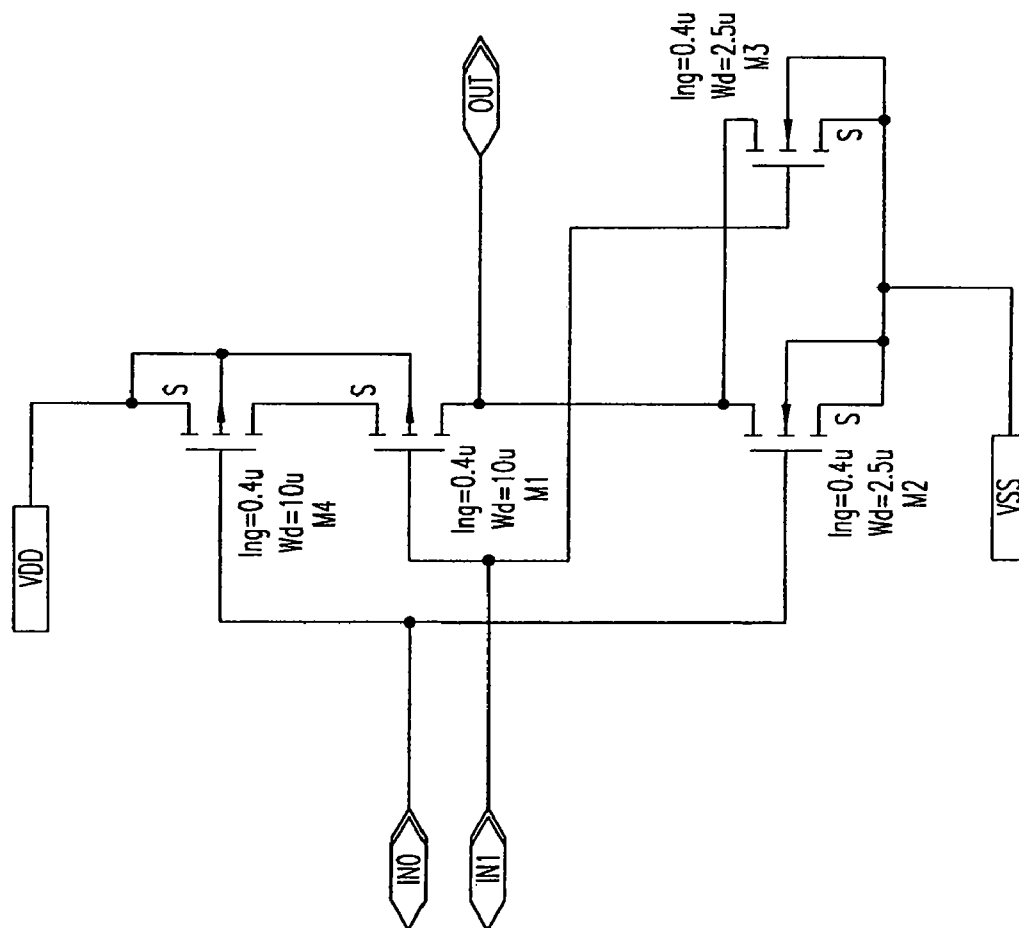


FIG. 132



**FIG. 133**



**FIG. 134**



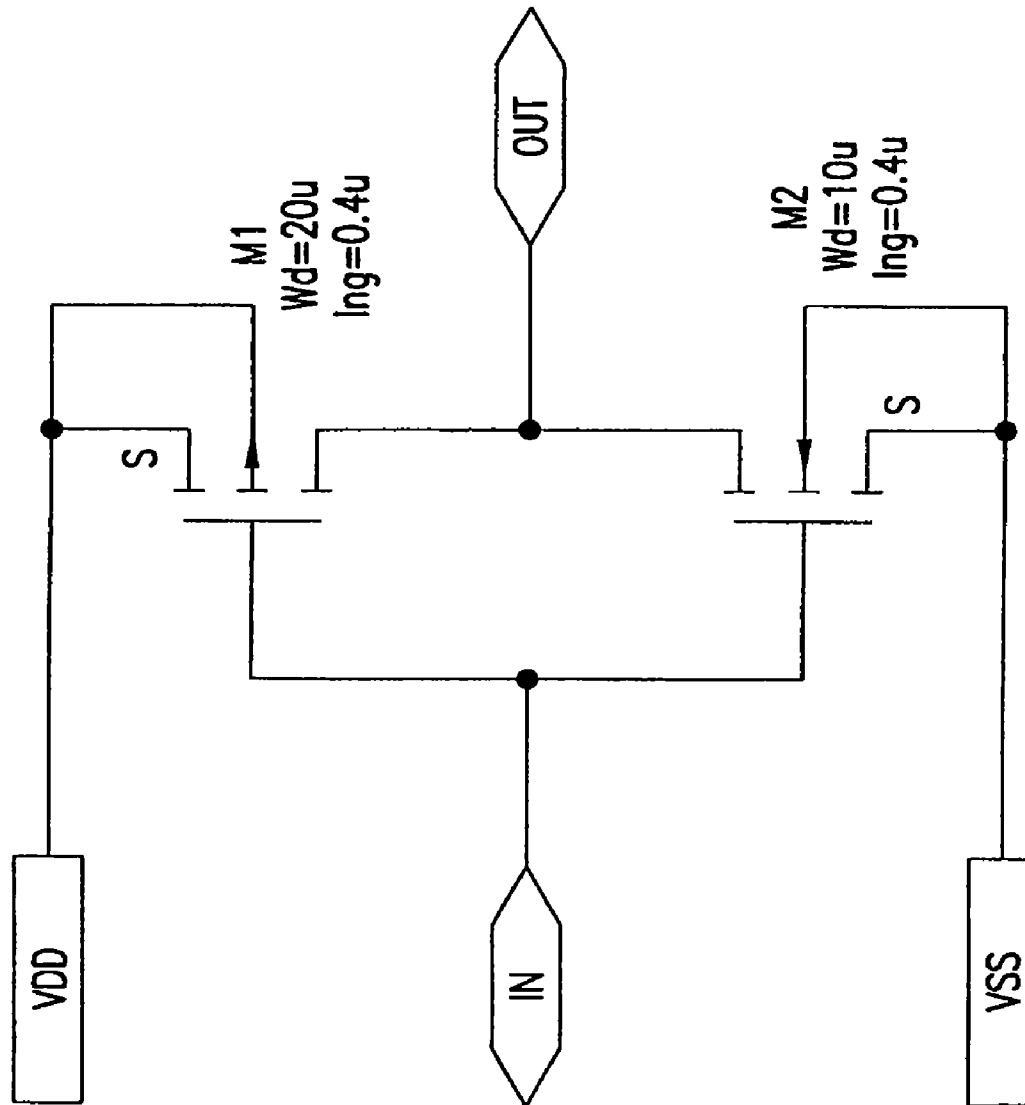
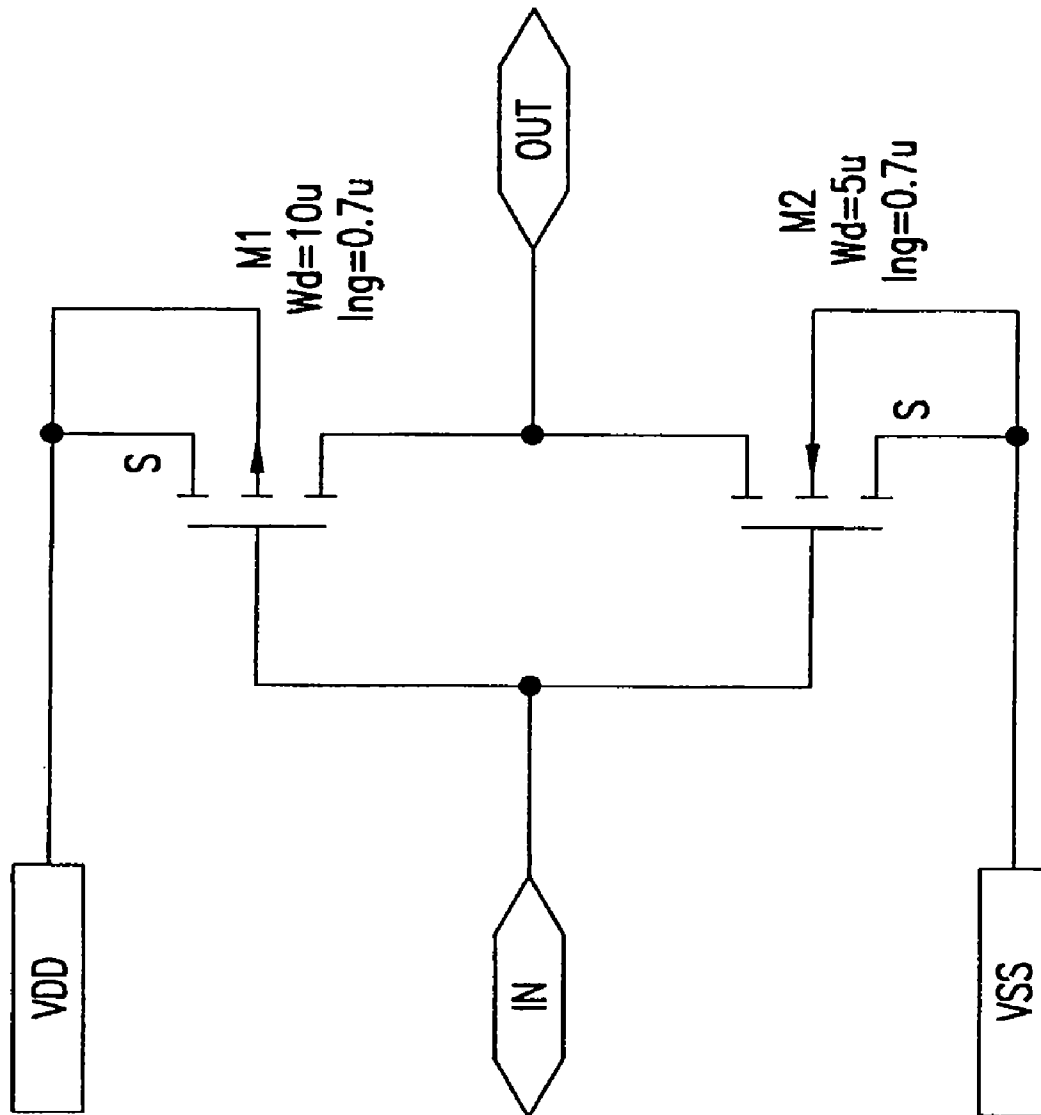


FIG. 135



**FIG. 136**

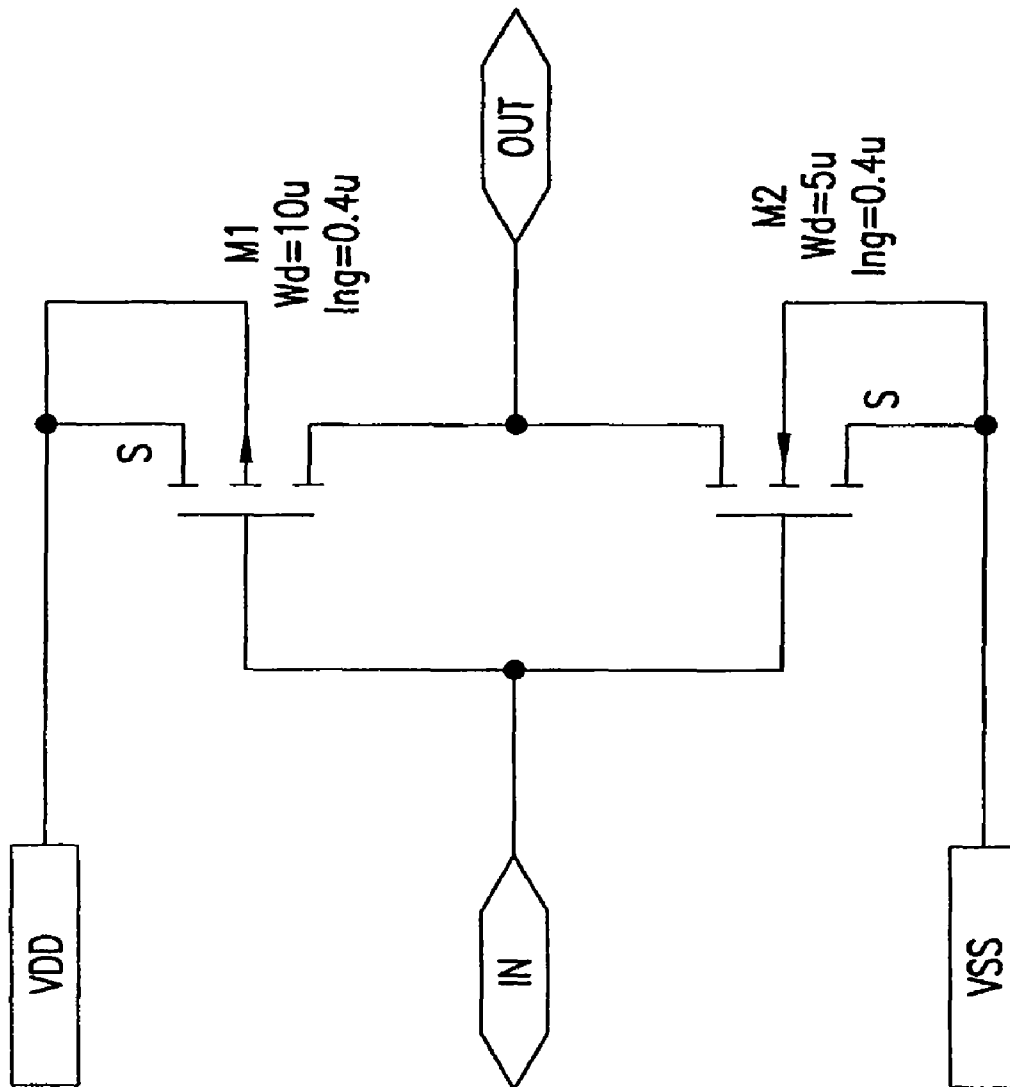


FIG.137

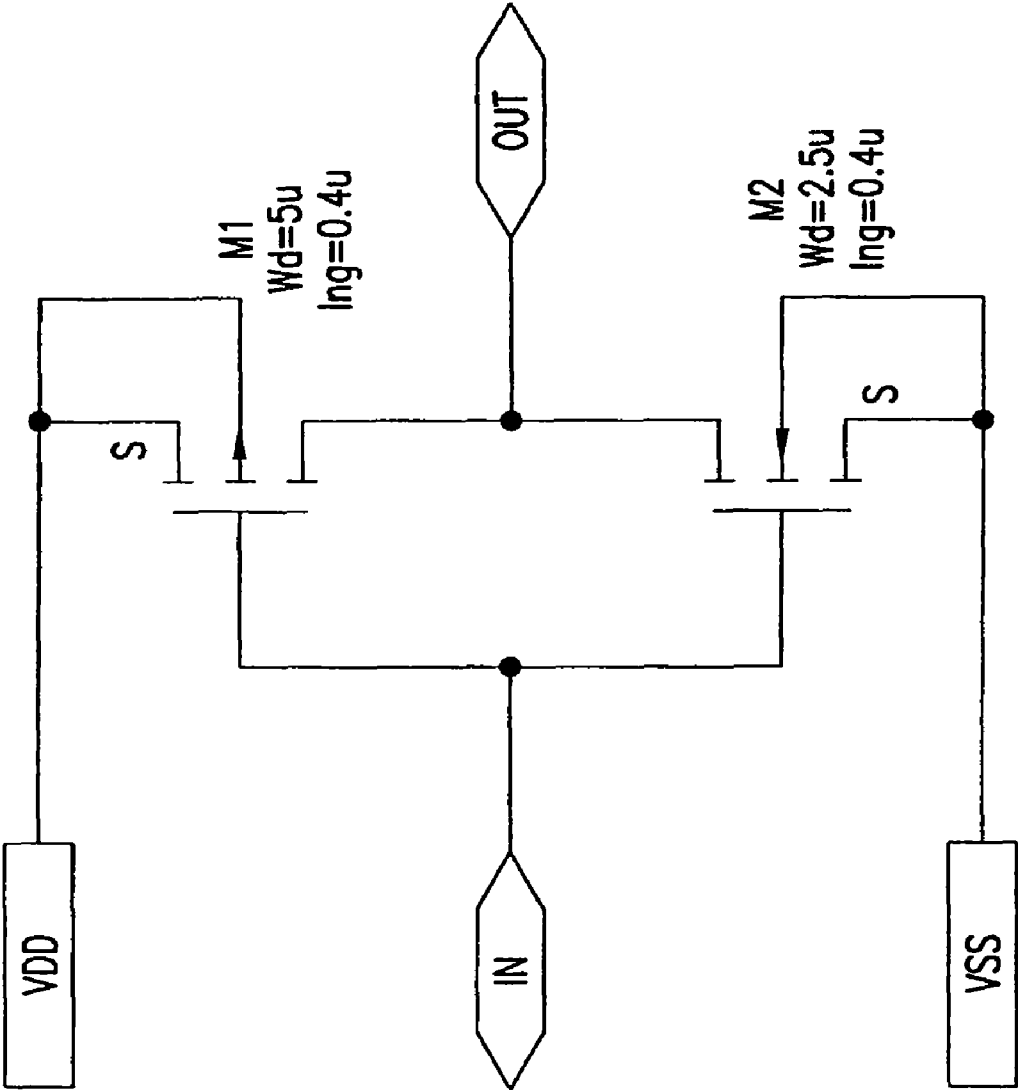


FIG.138

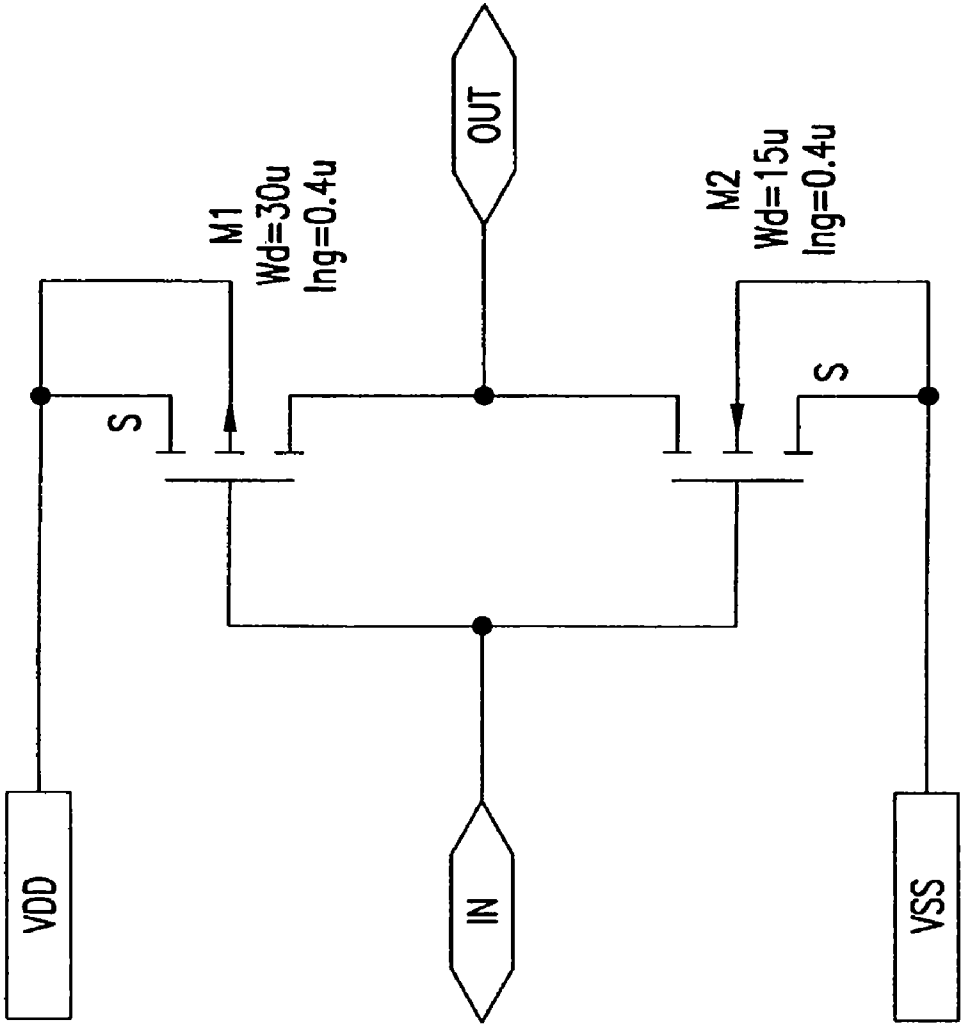


FIG. 139

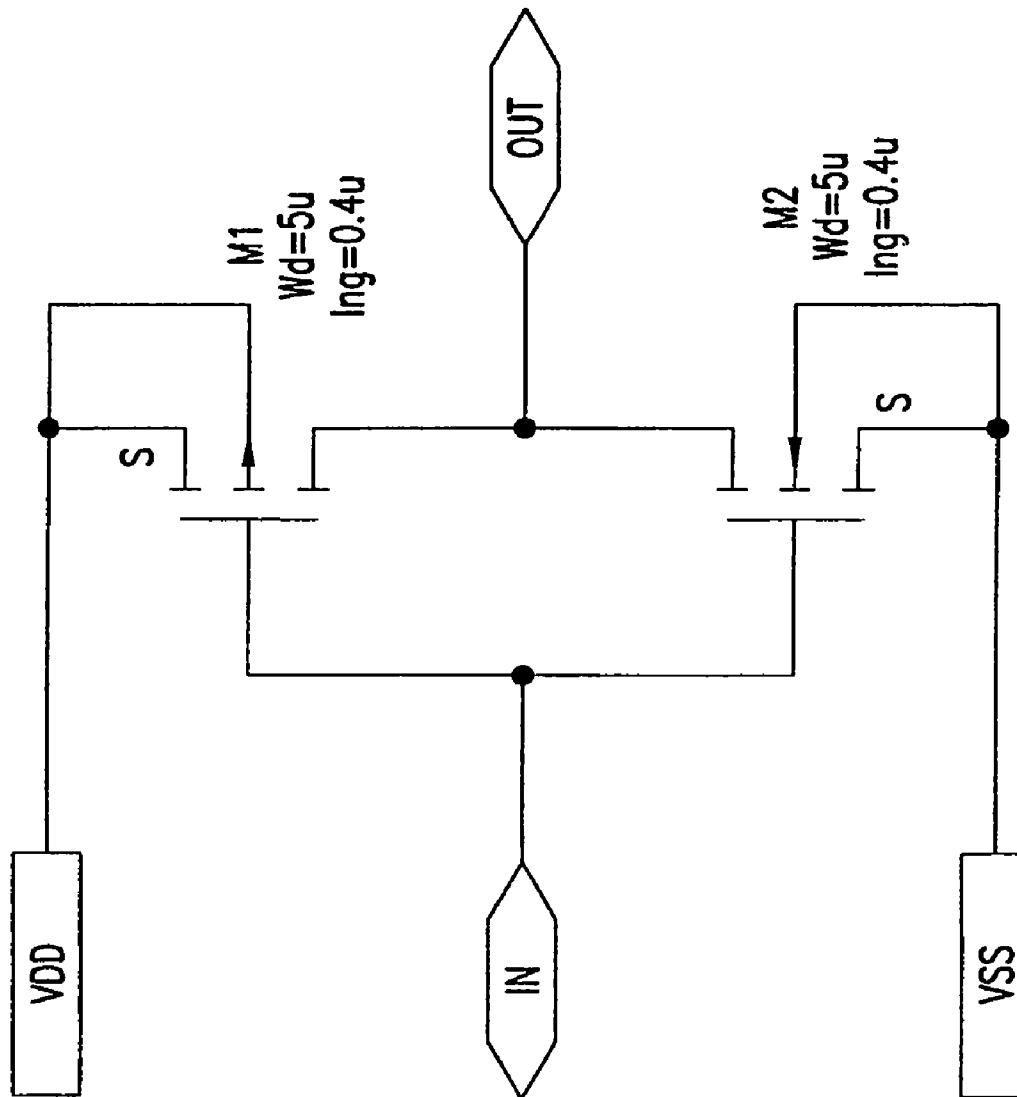


FIG. 140

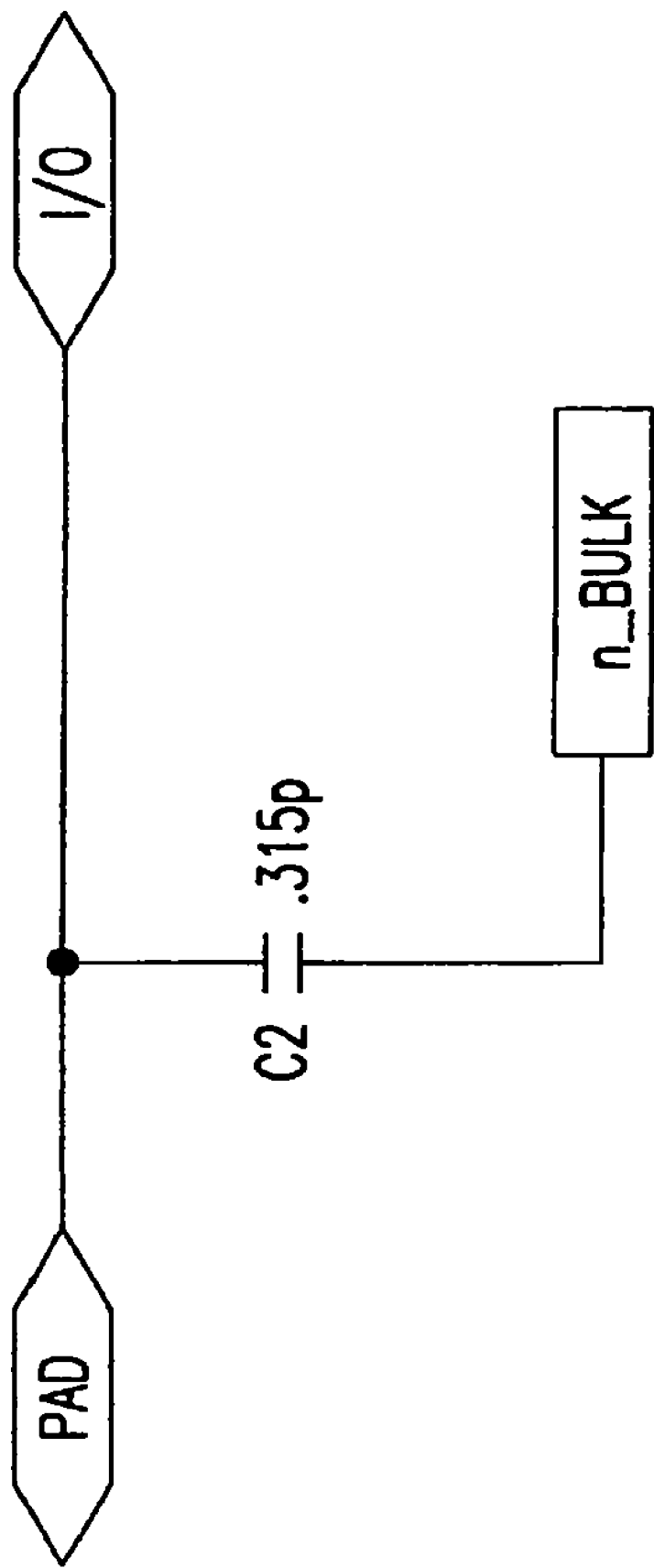


FIG.141

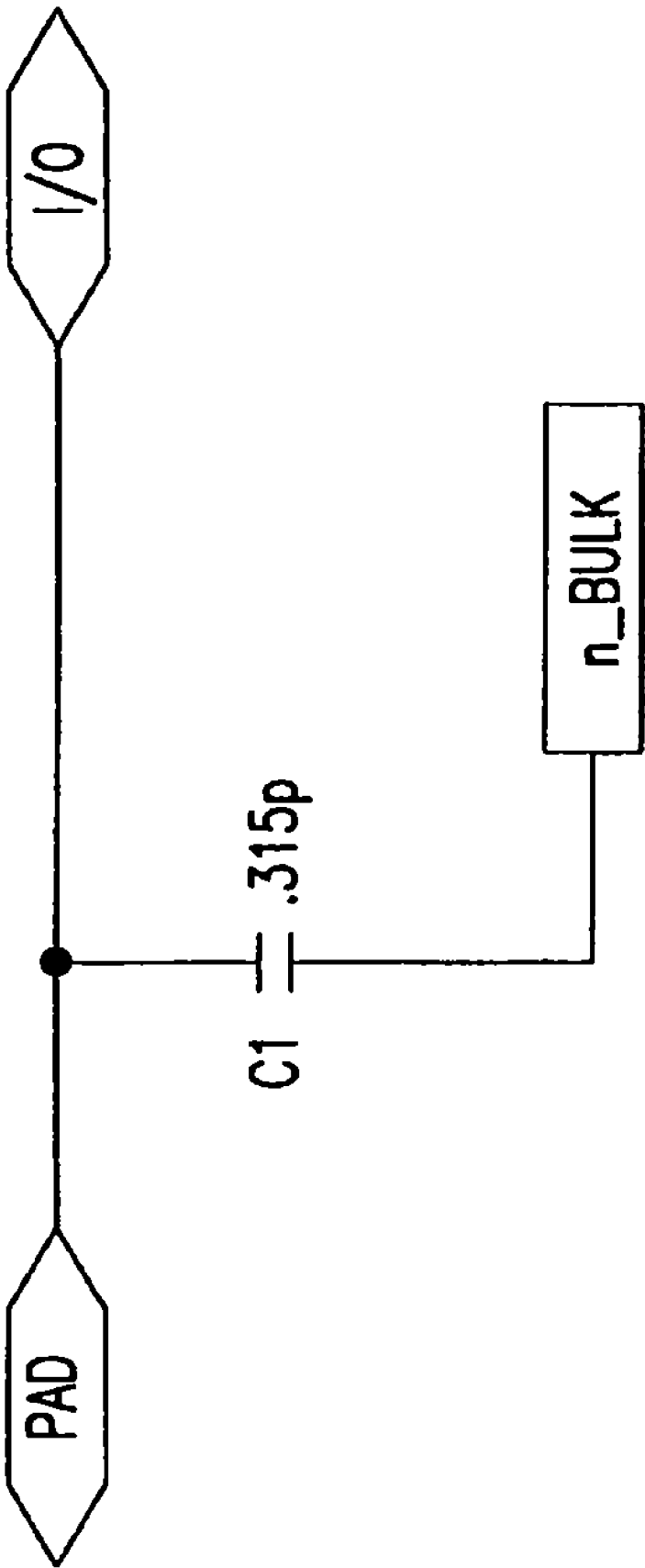


FIG. 142



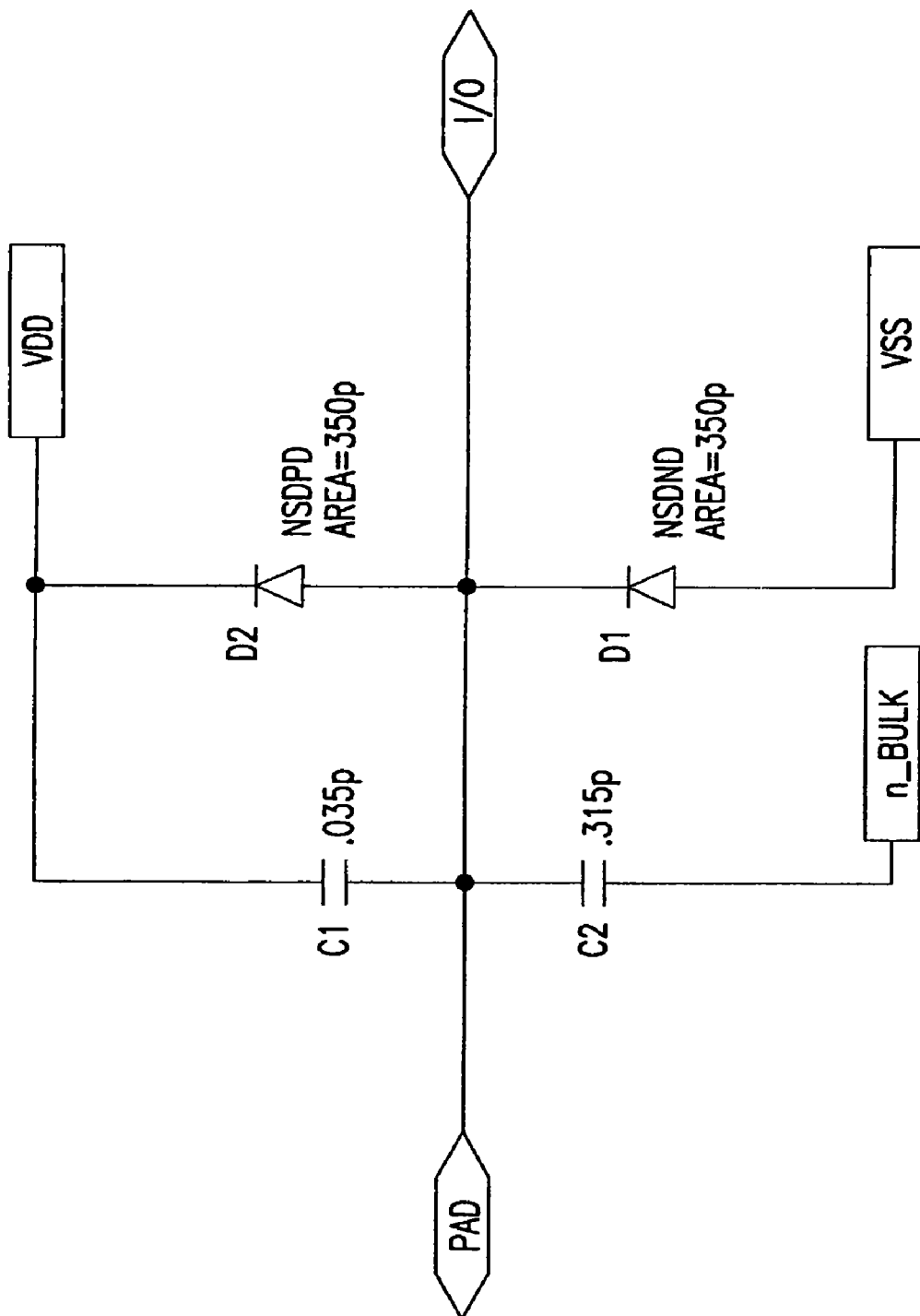


FIG.143

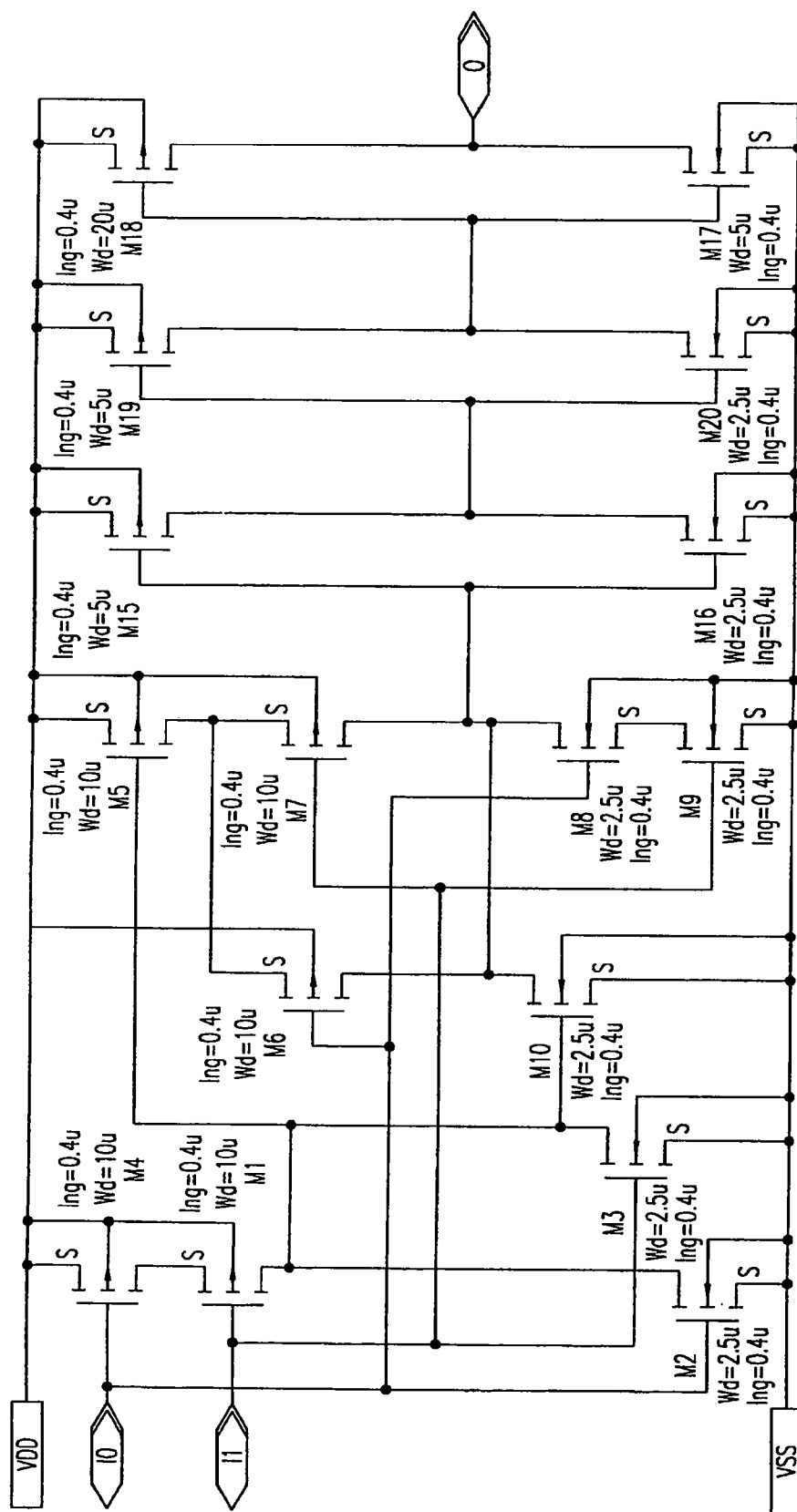


FIG. 144

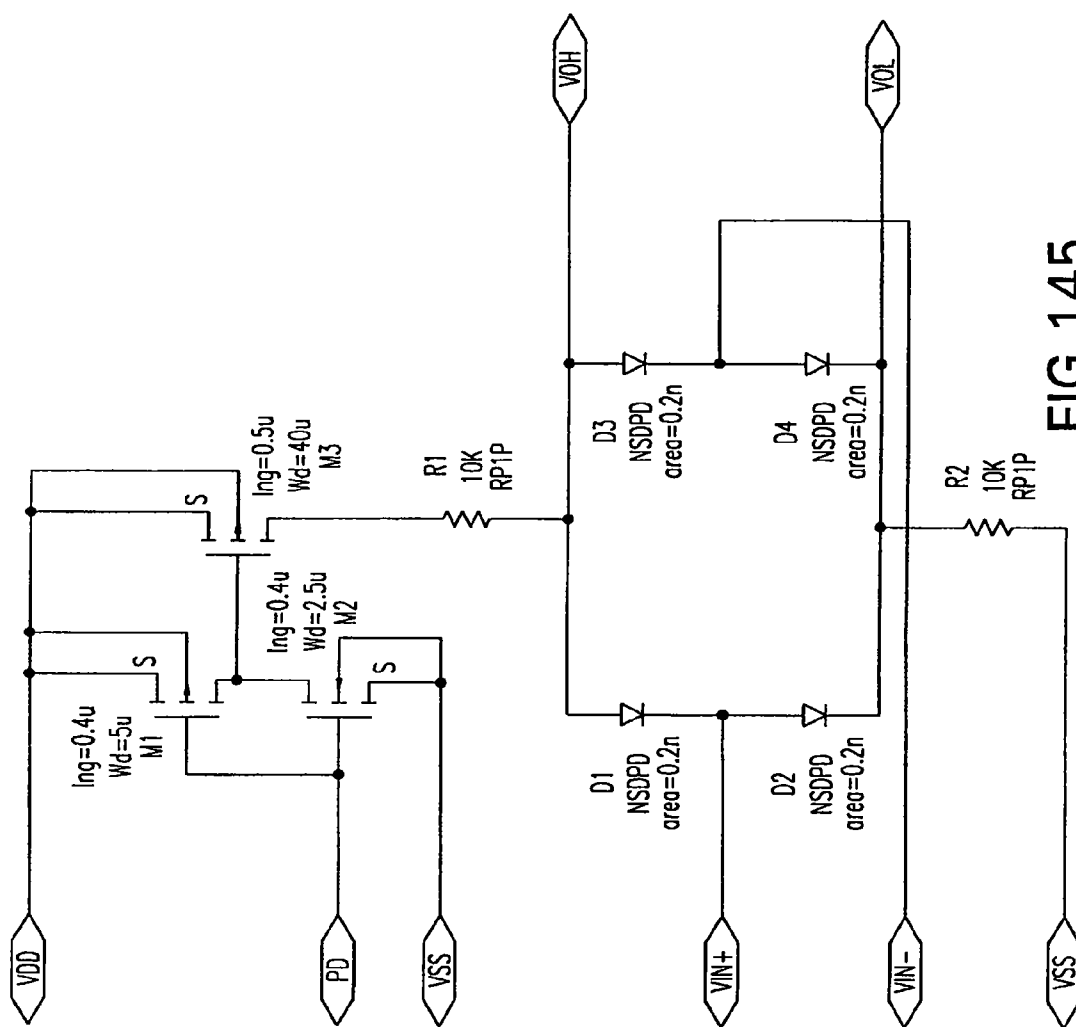


FIG. 145

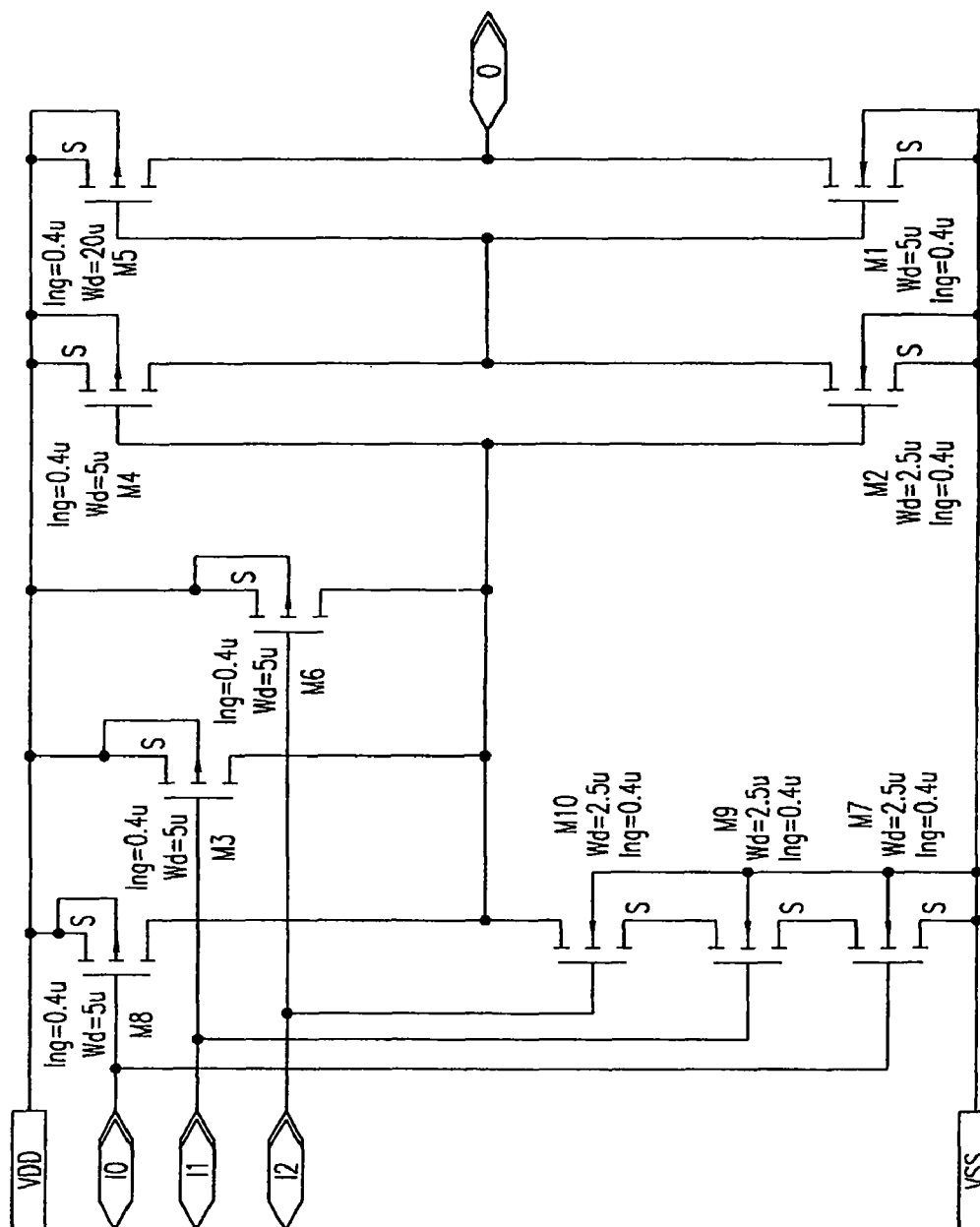


FIG. 146

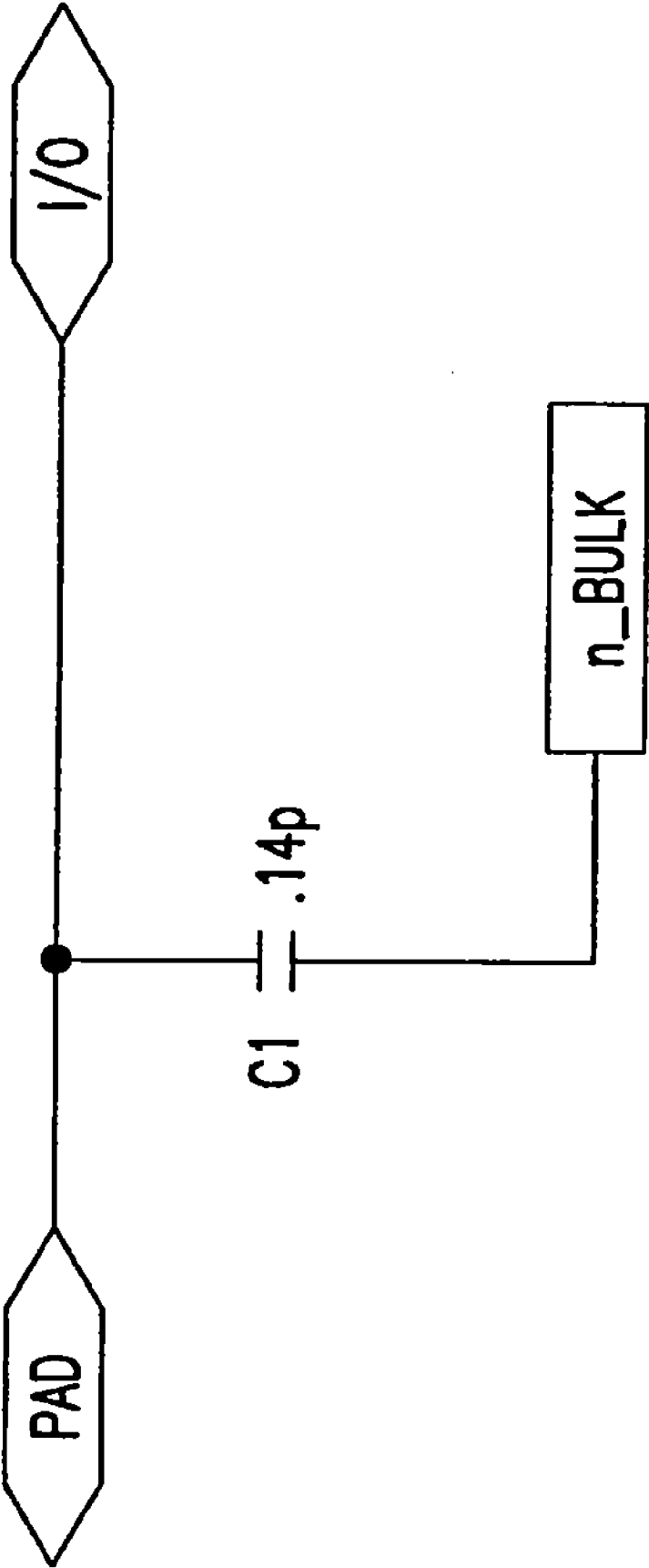


FIG.147

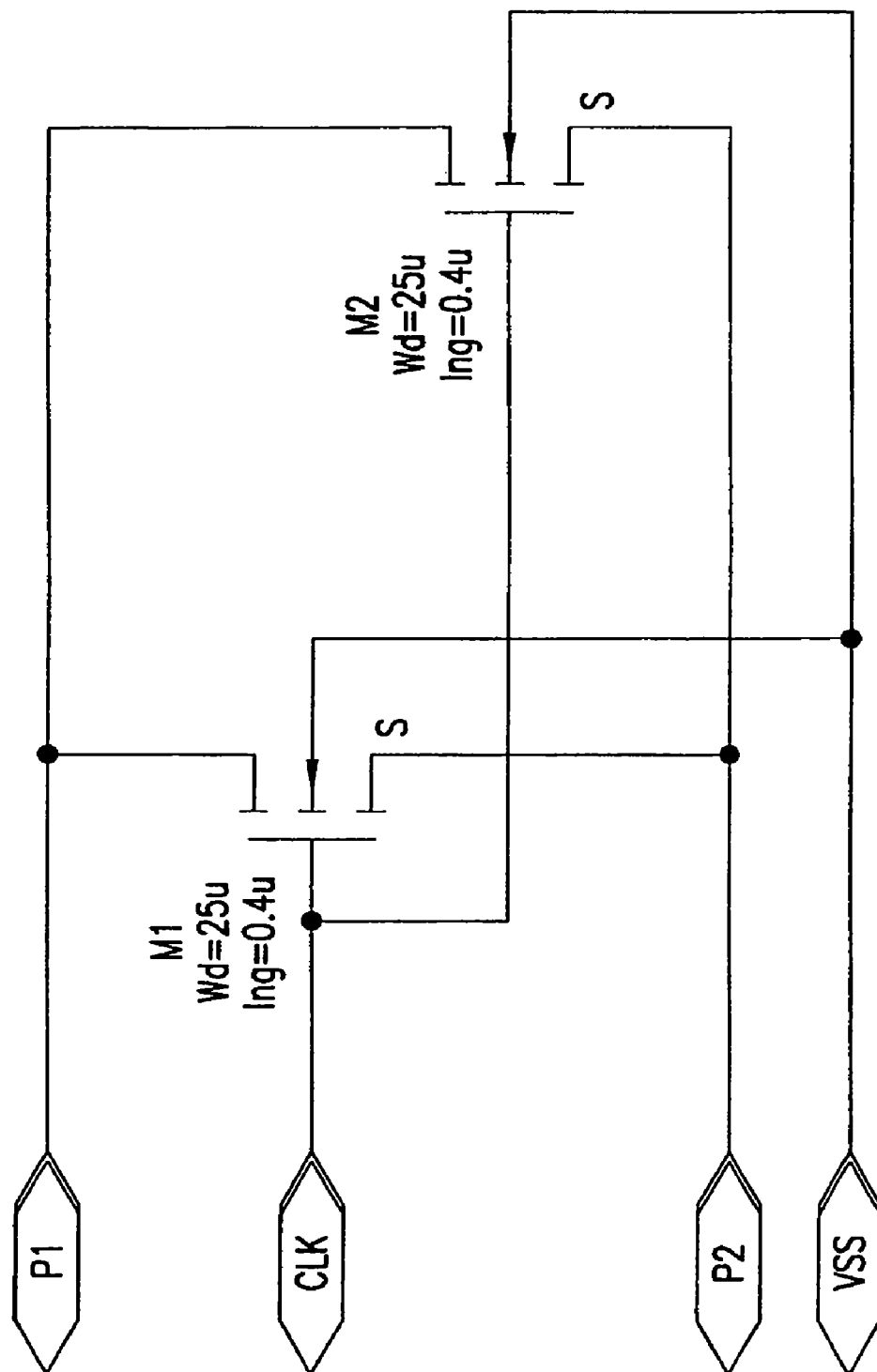


FIG. 148

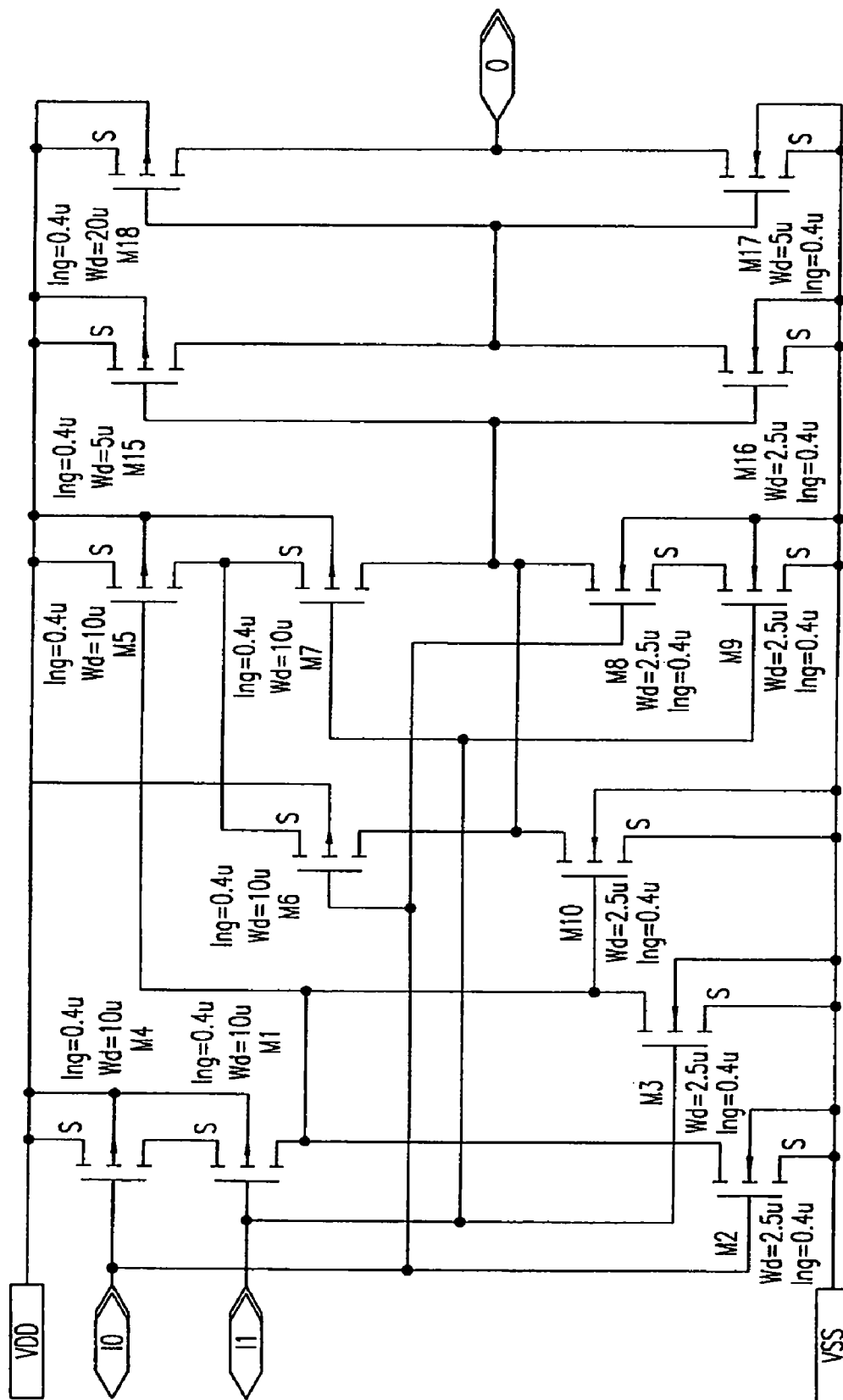


FIG. 149

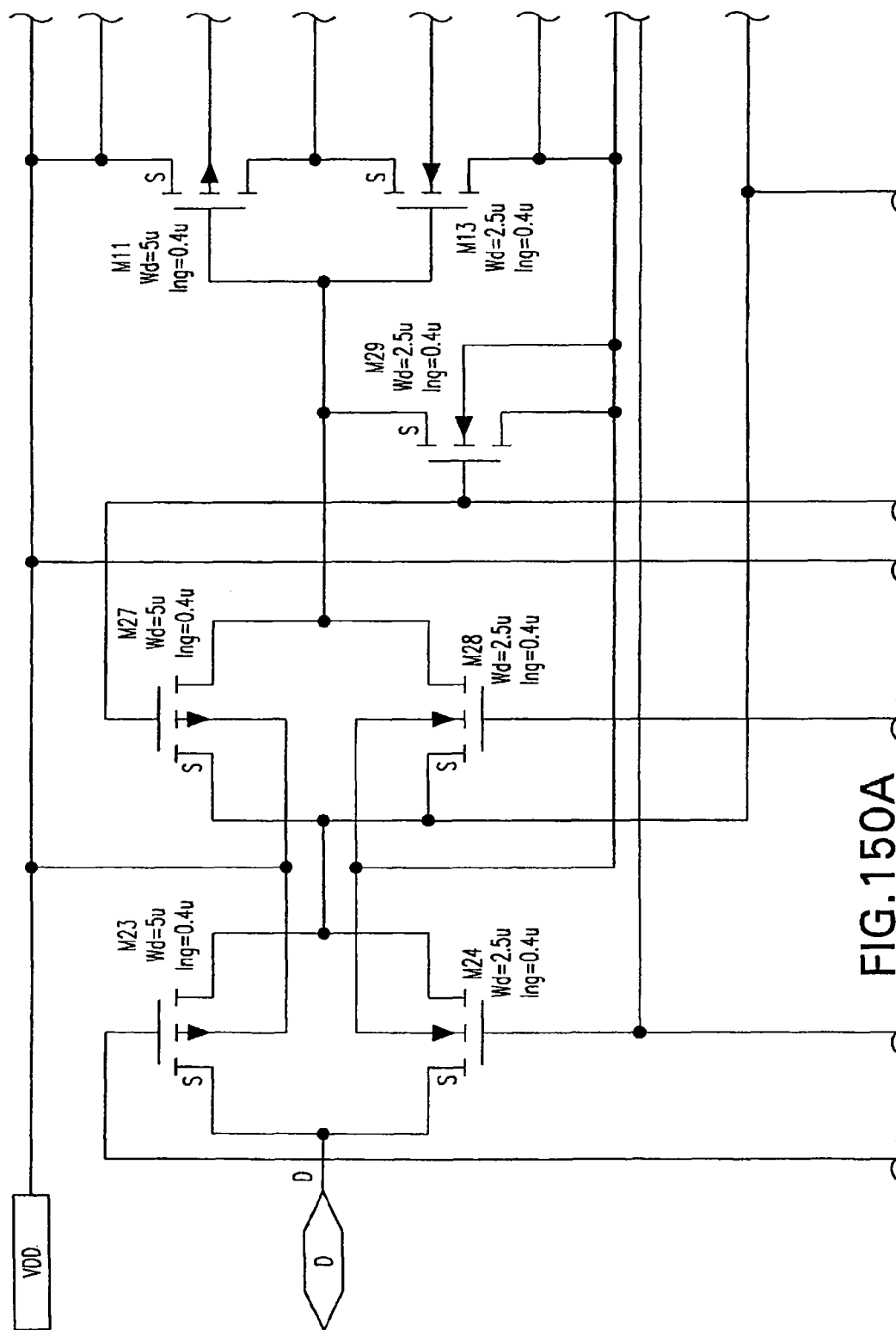
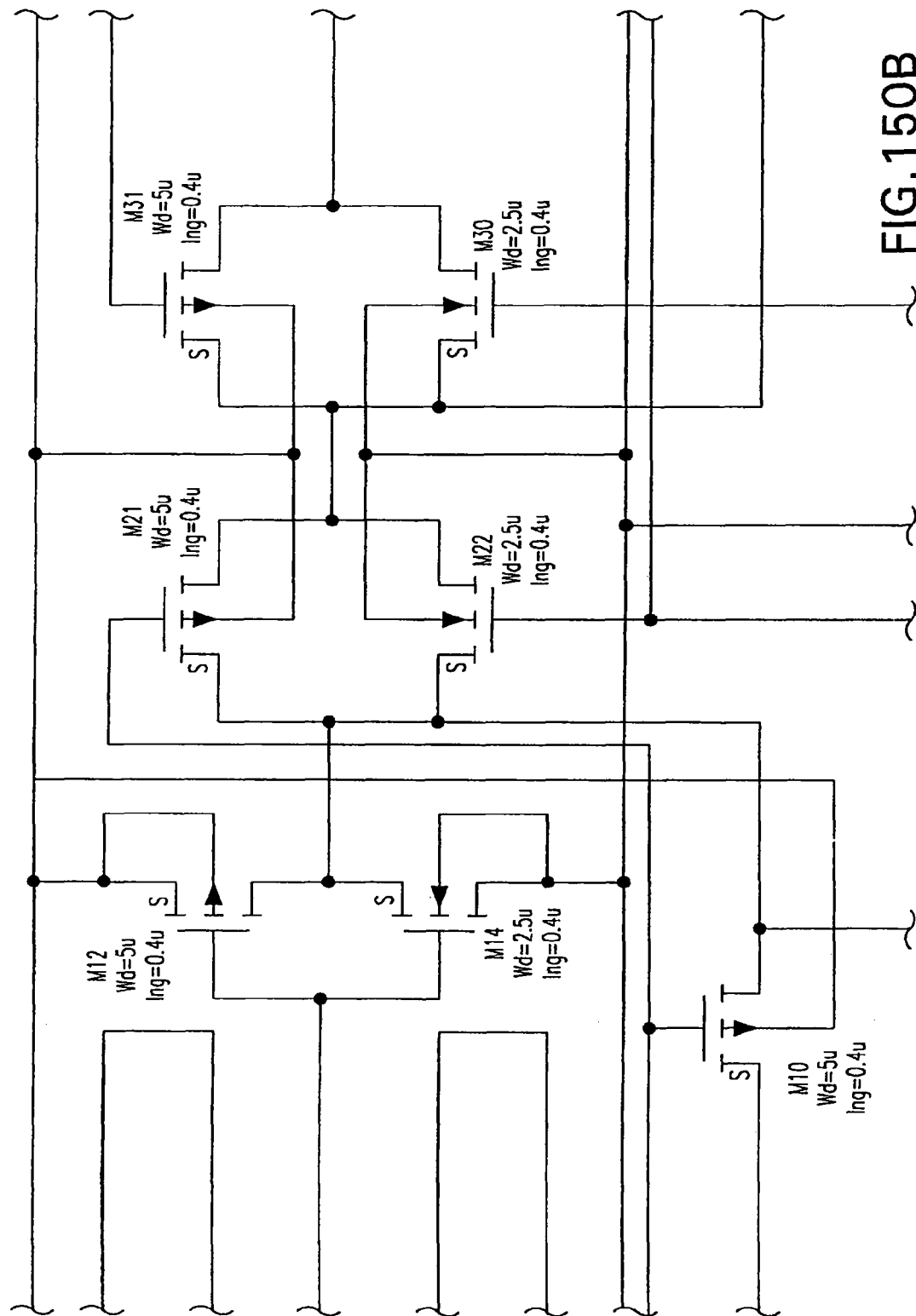


FIG. 150A





**FIG. 150B**

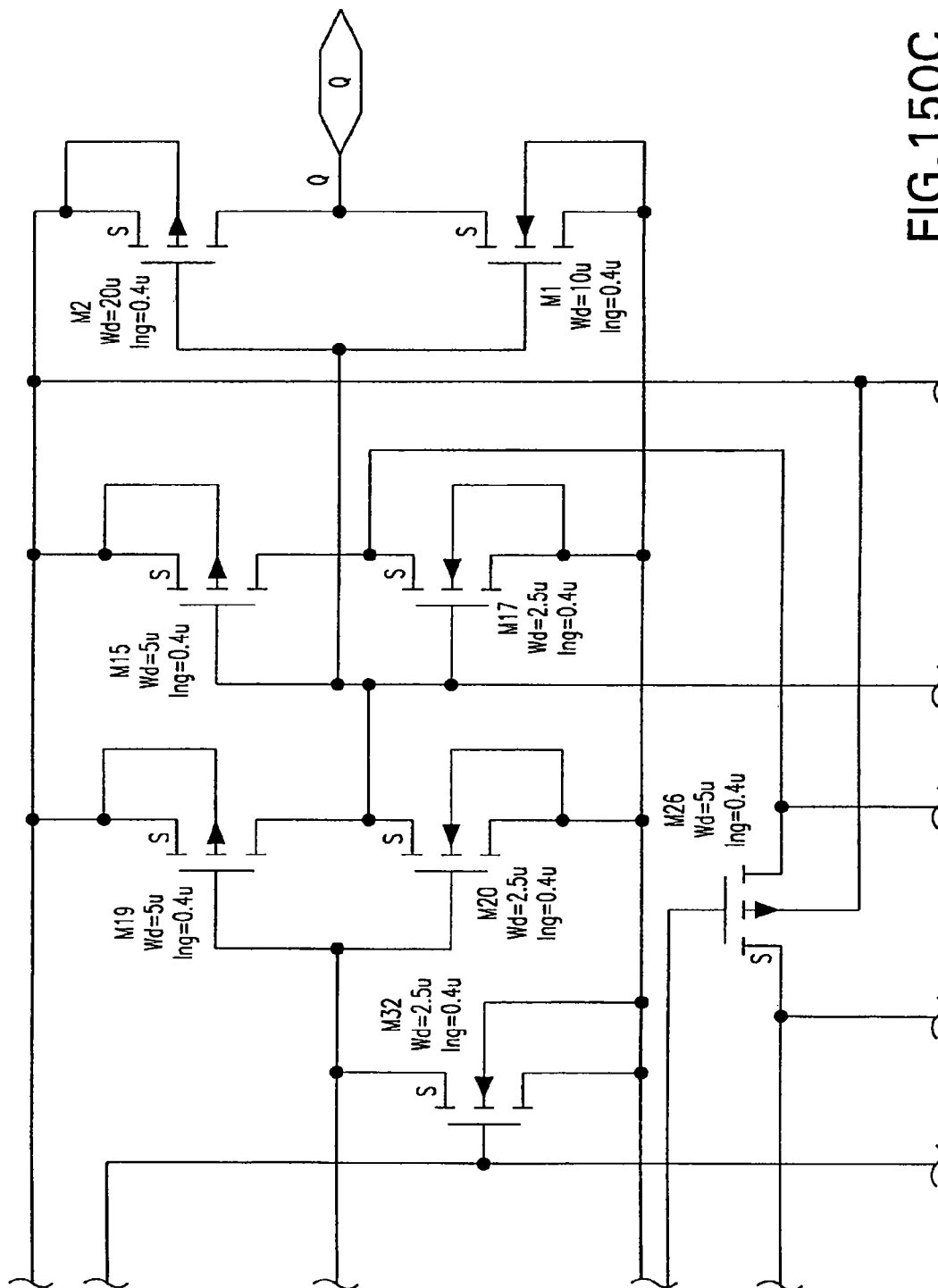
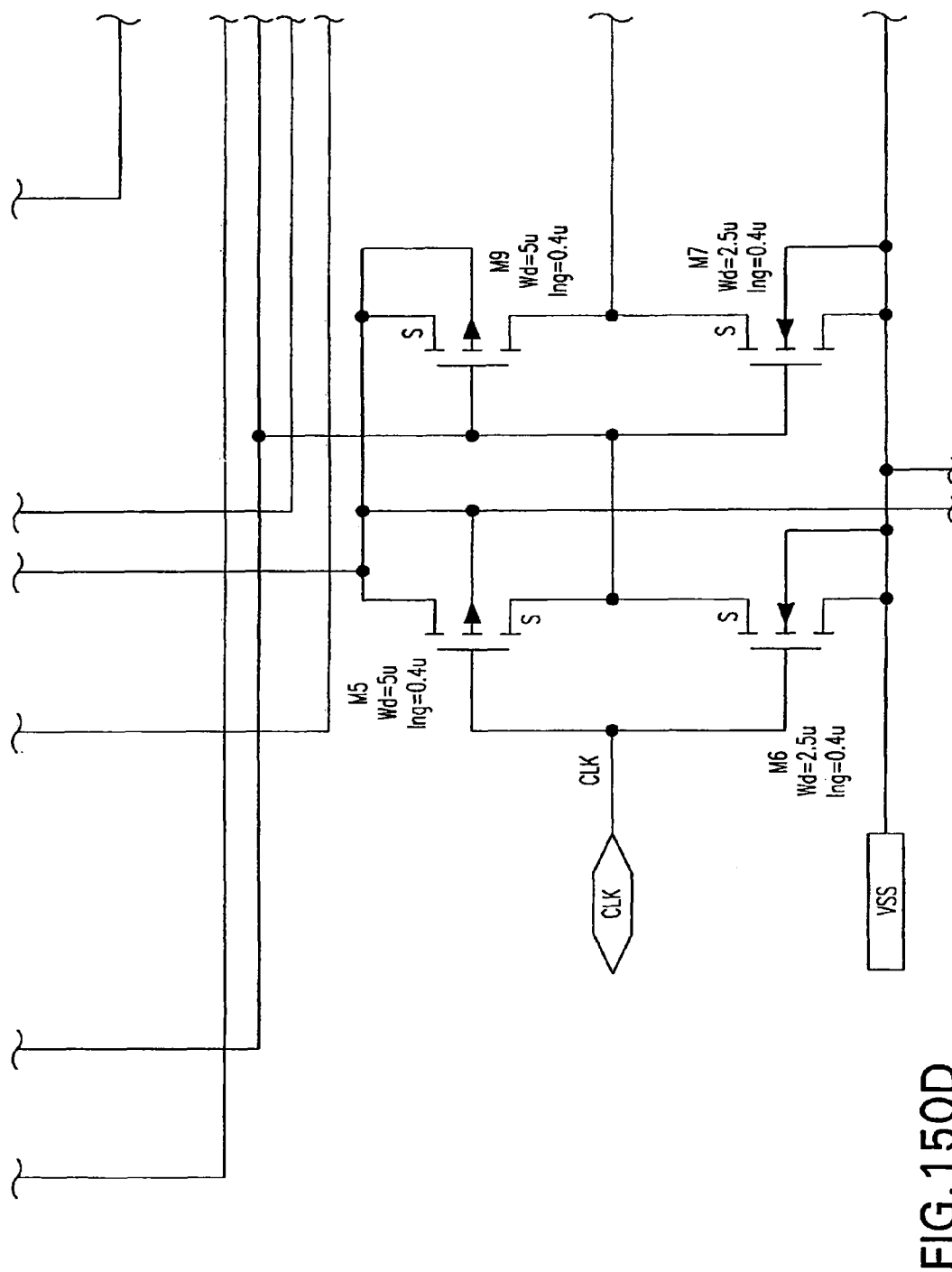
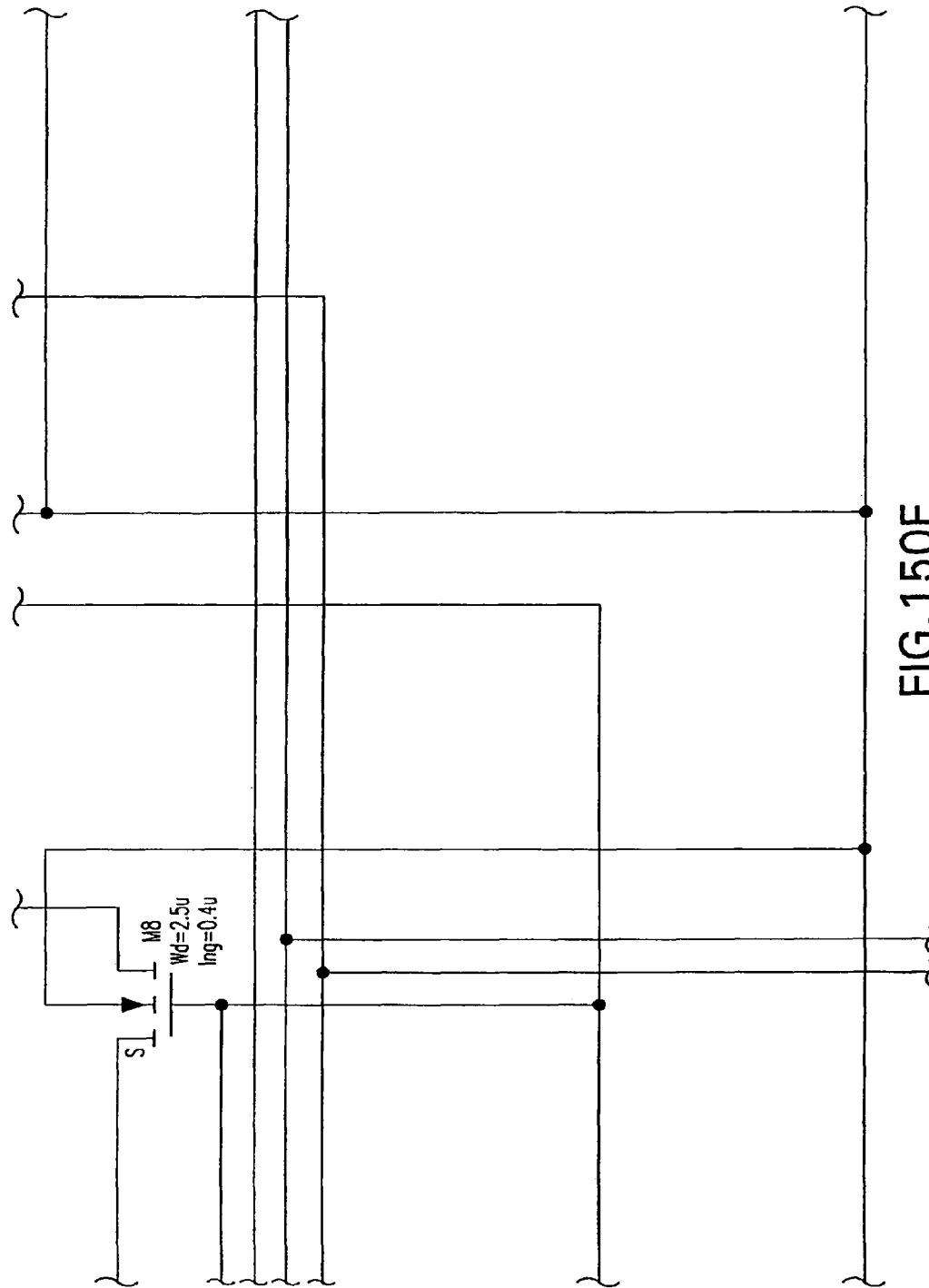


FIG. 150C





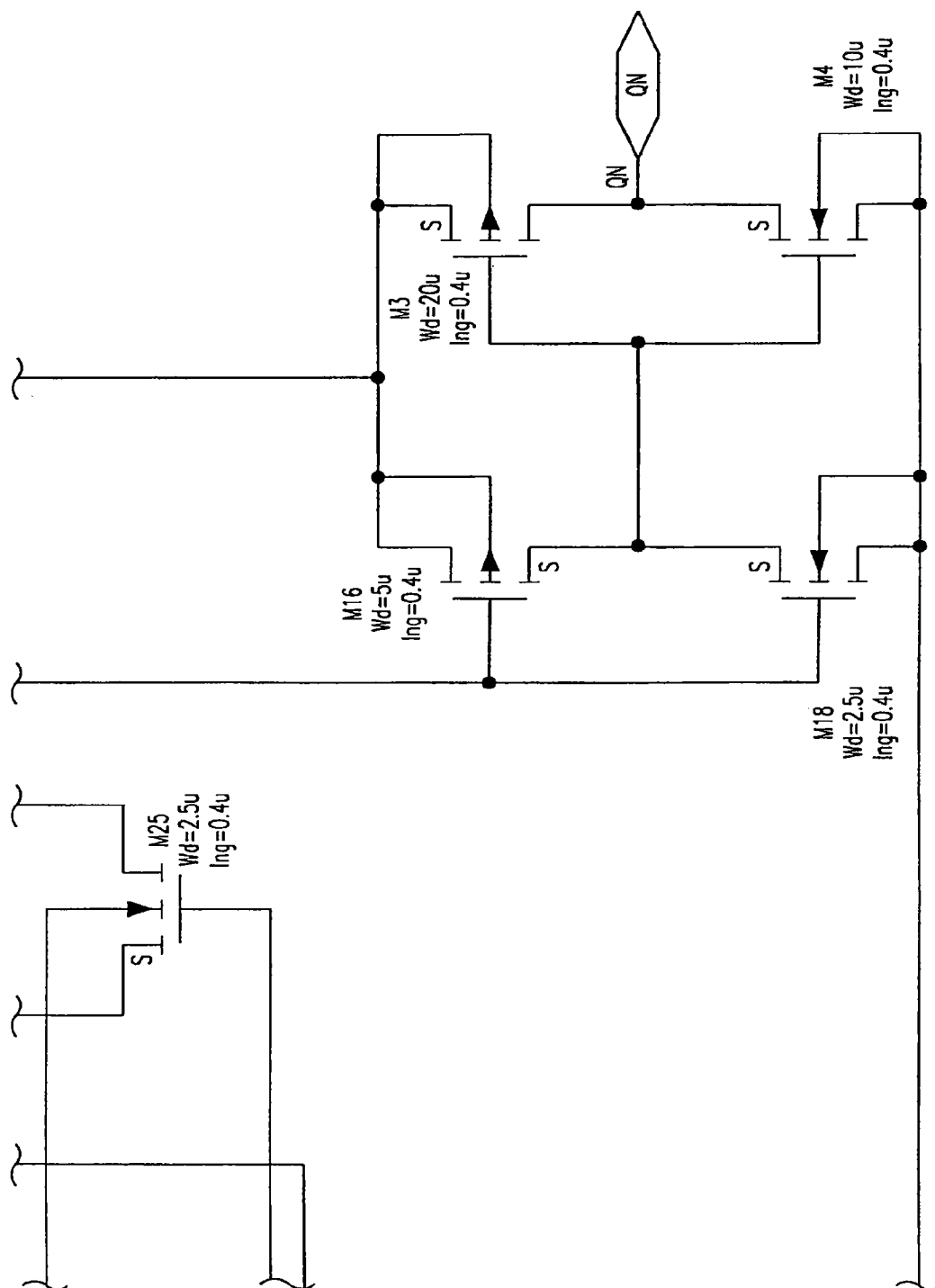


FIG. 150F

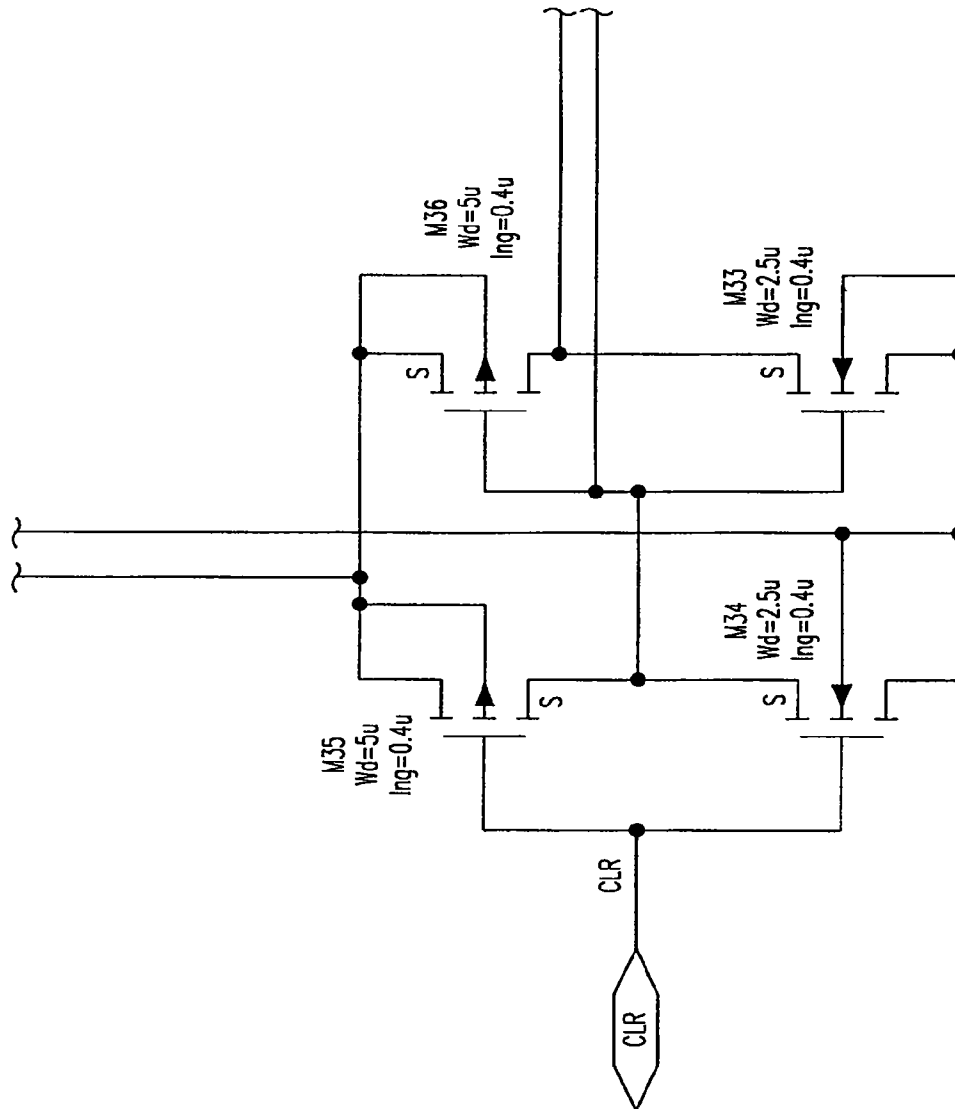


FIG. 150G

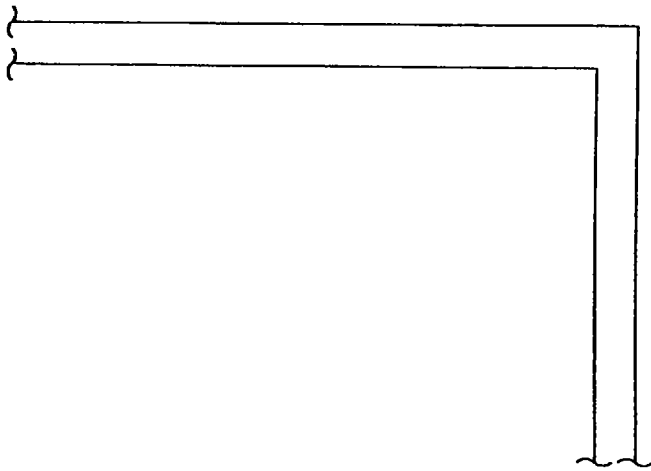


FIG. 150H

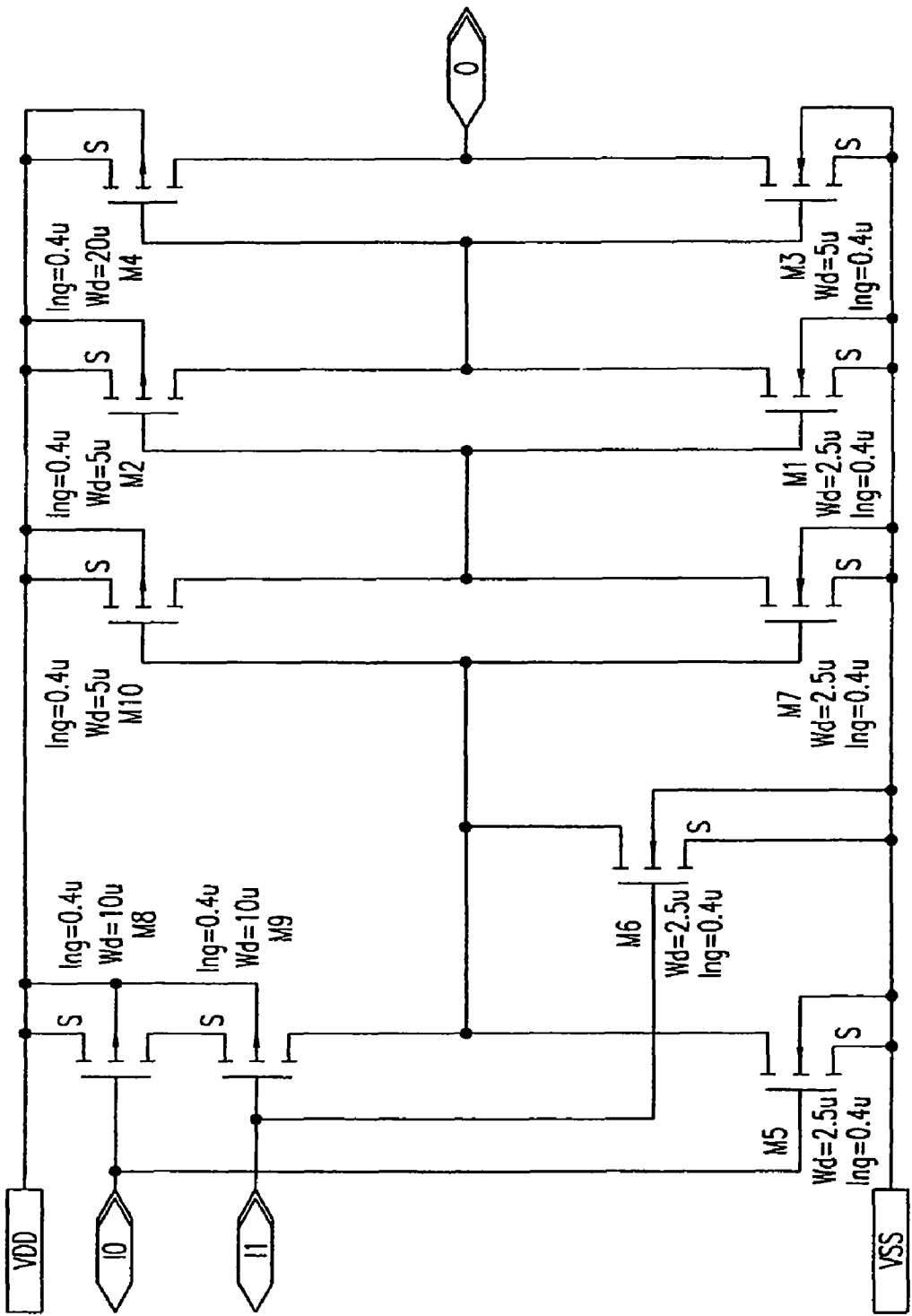


FIG.151



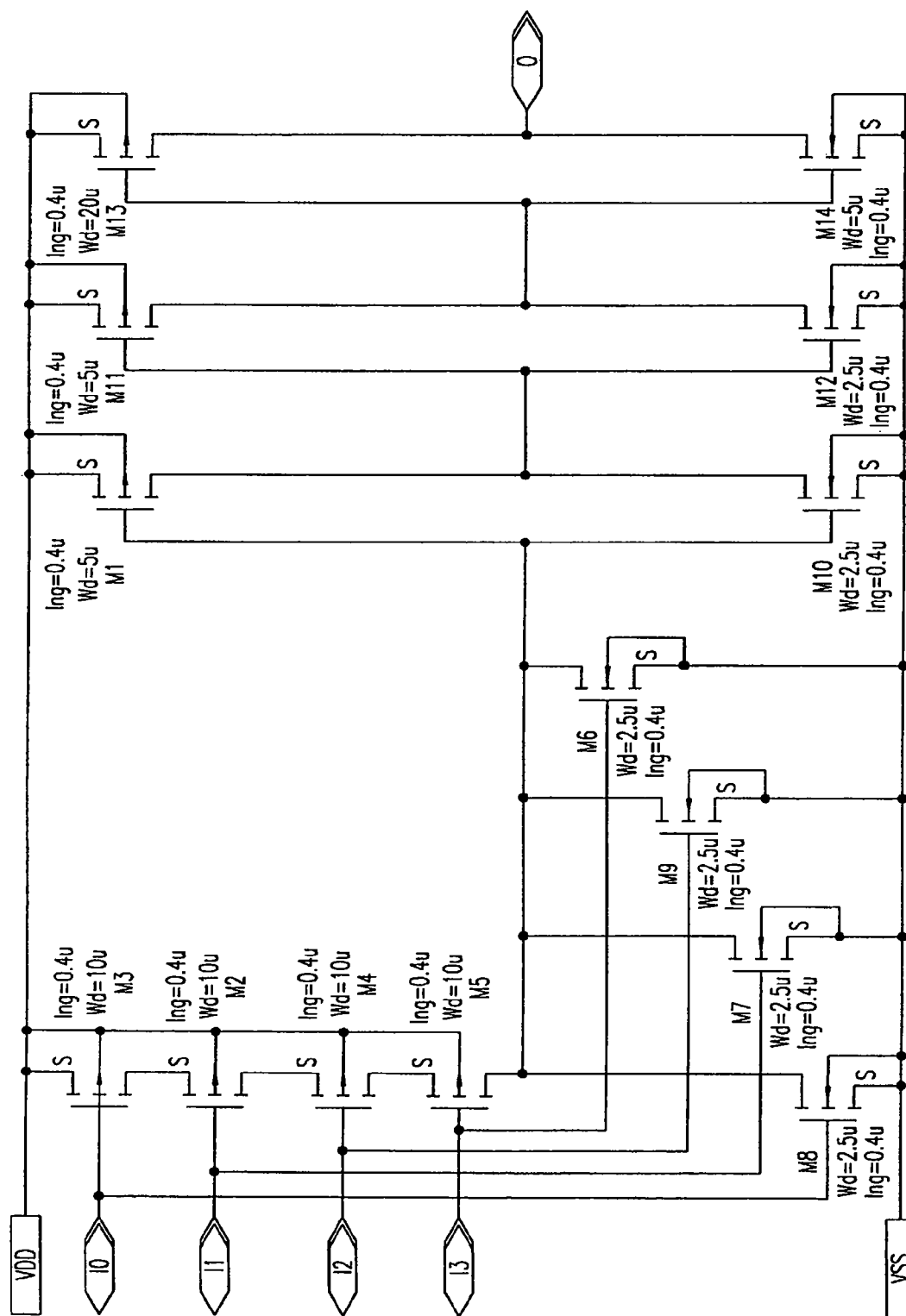


FIG. 152

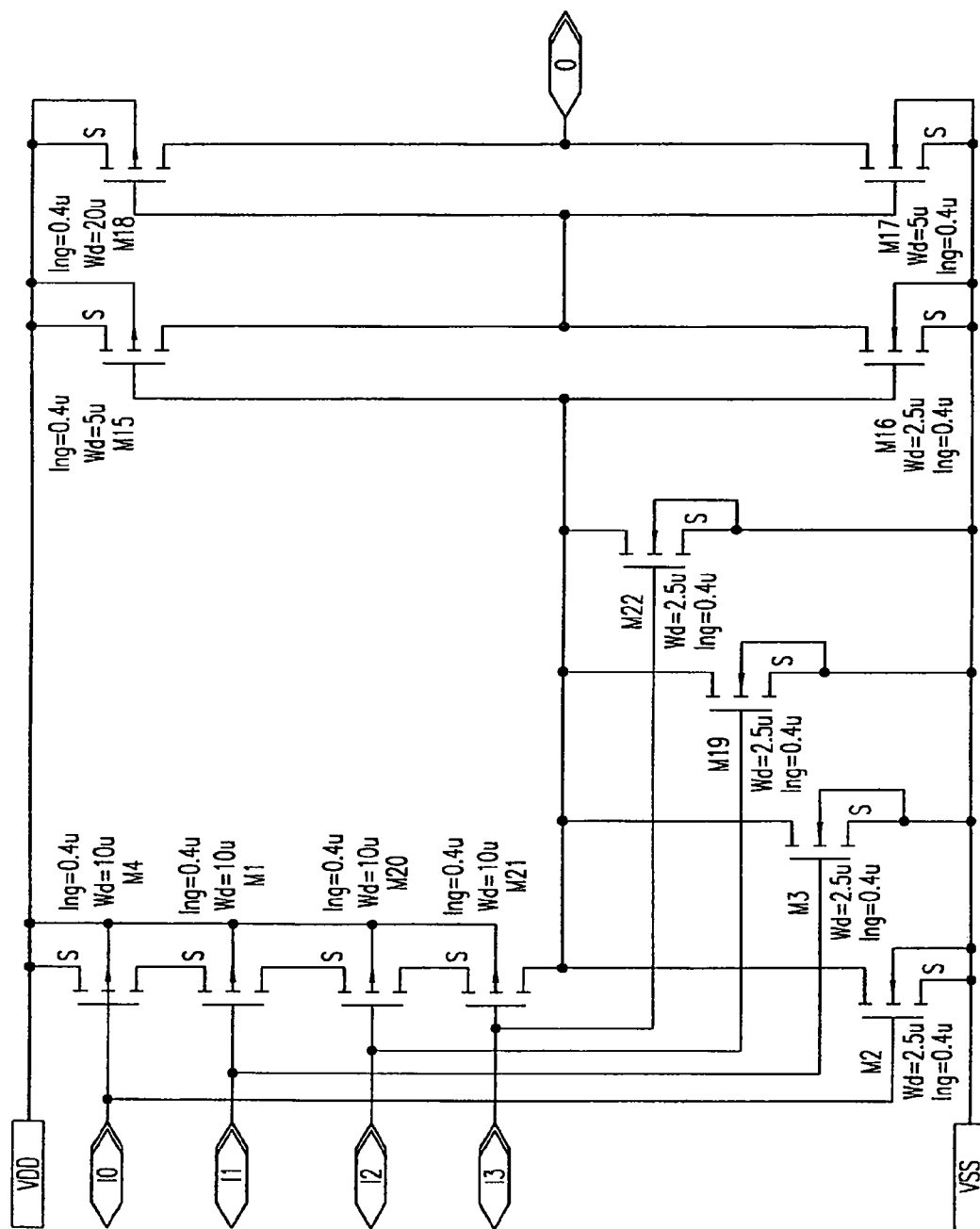


FIG.153

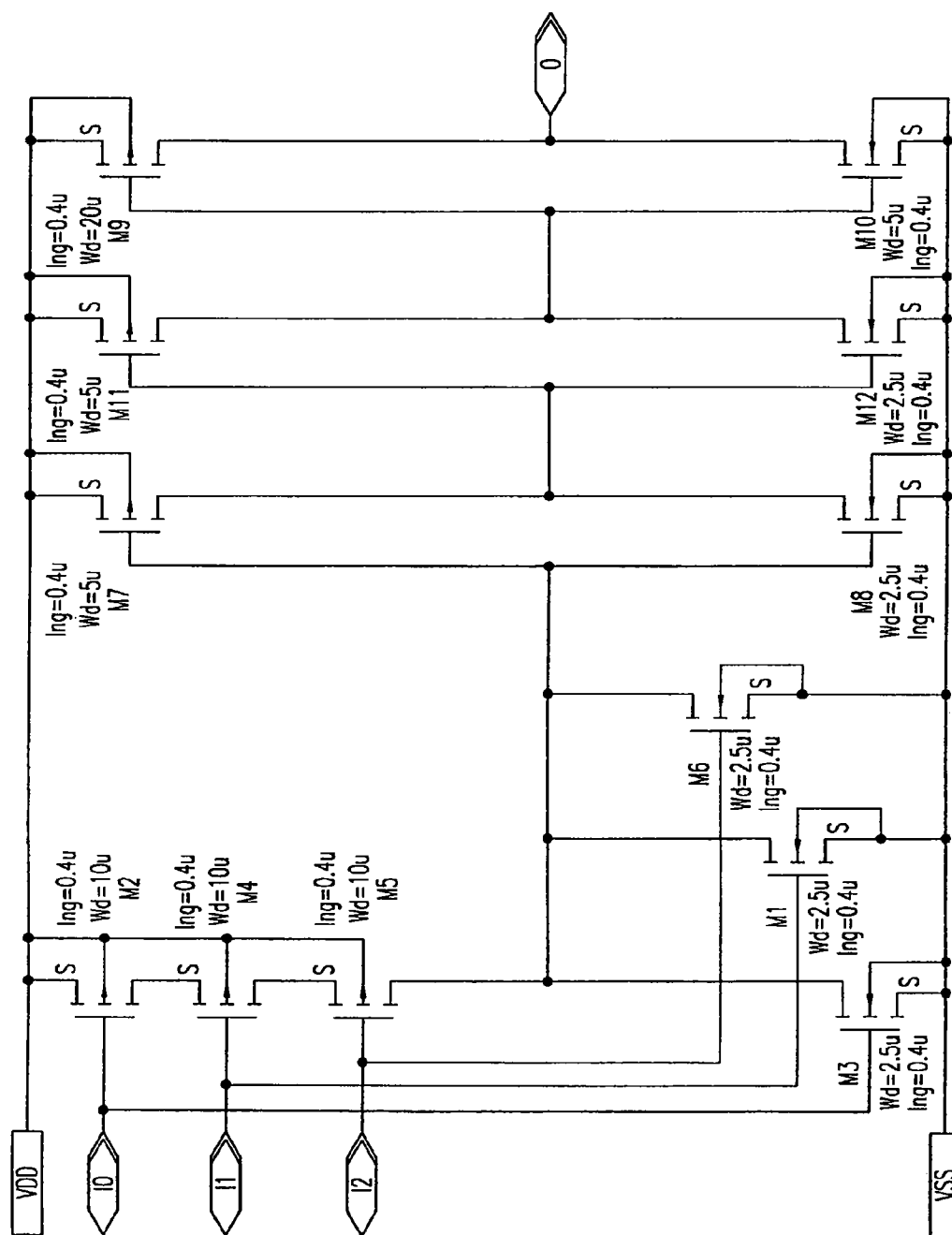


FIG.154

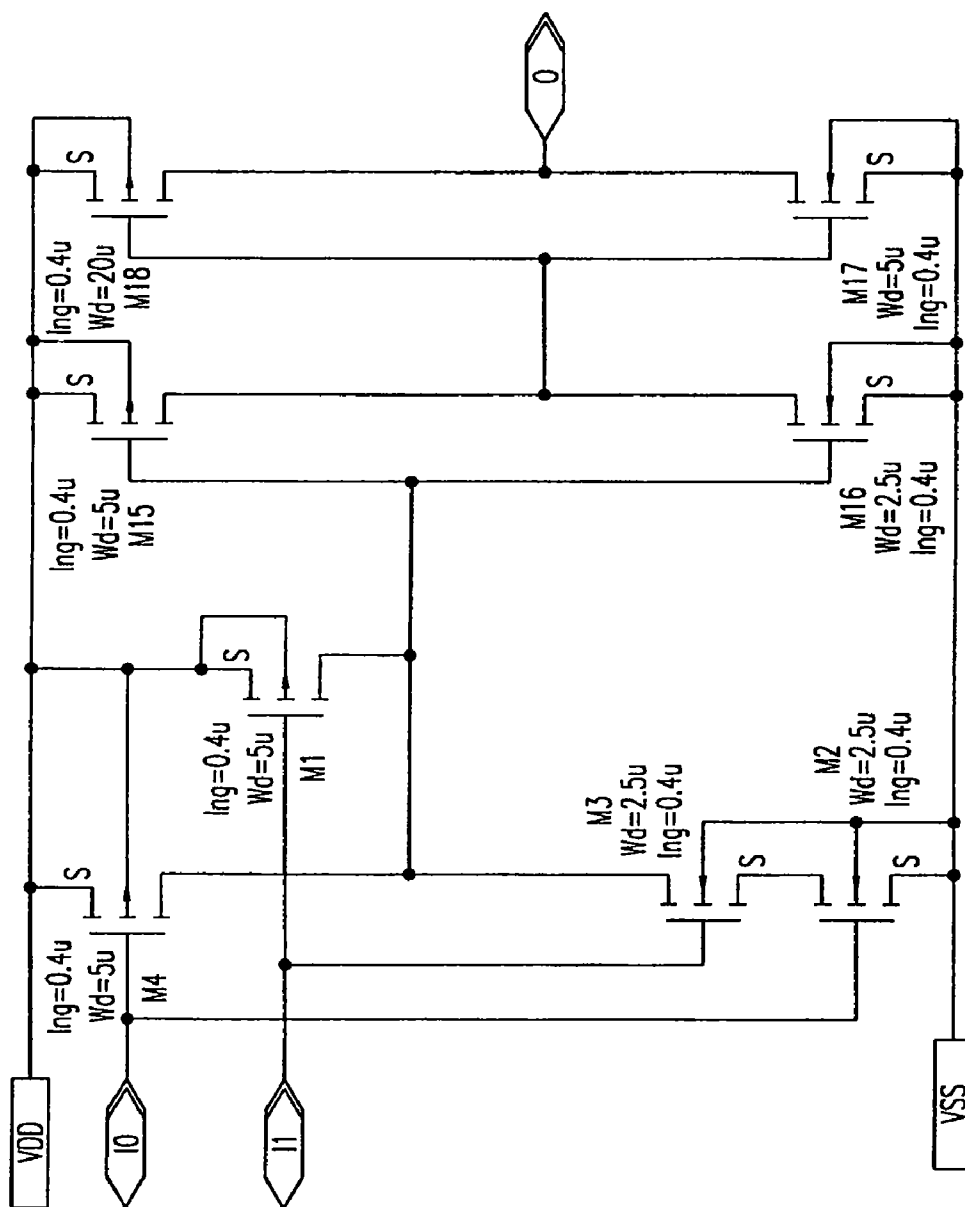


FIG. 155

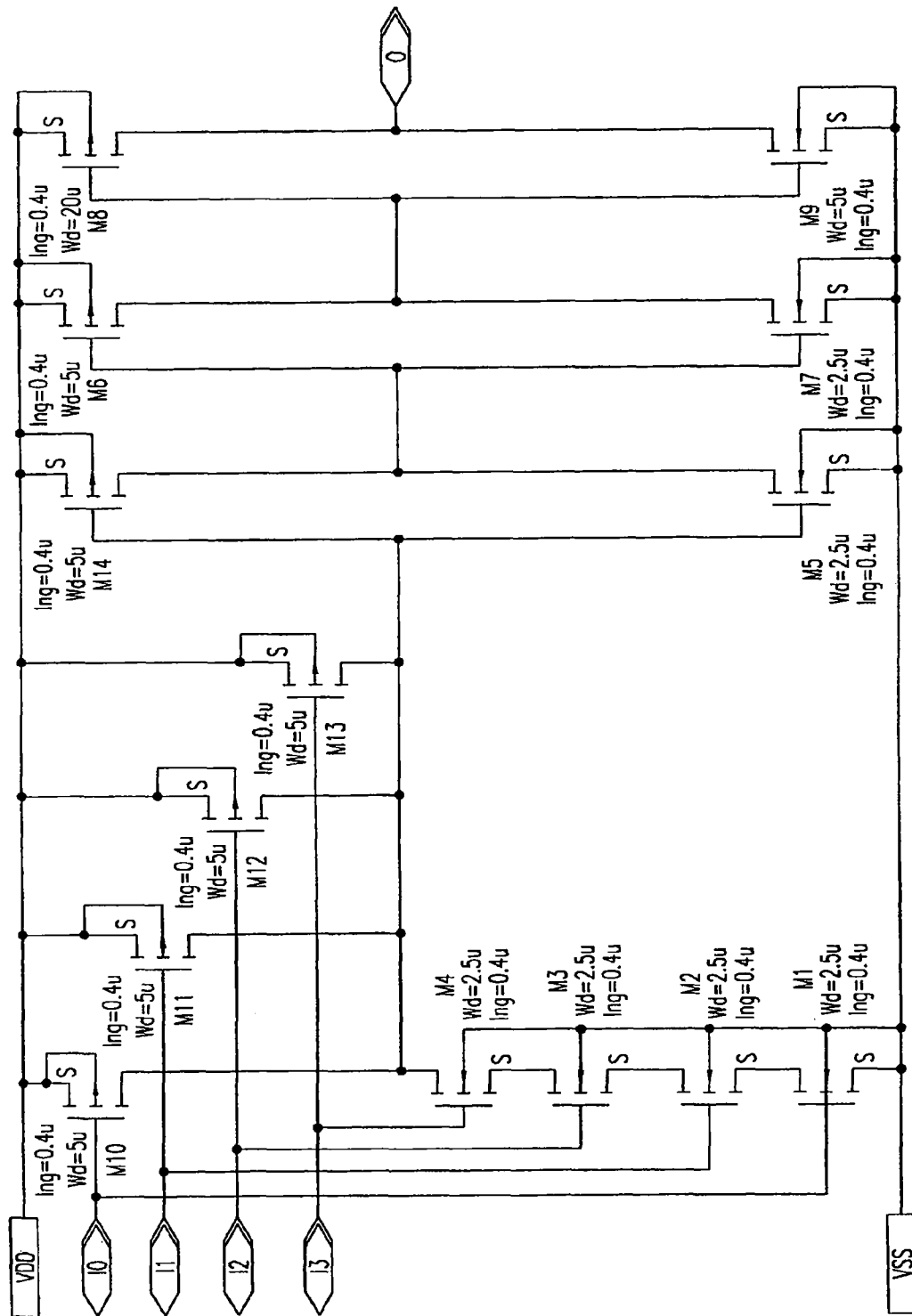


FIG. 156

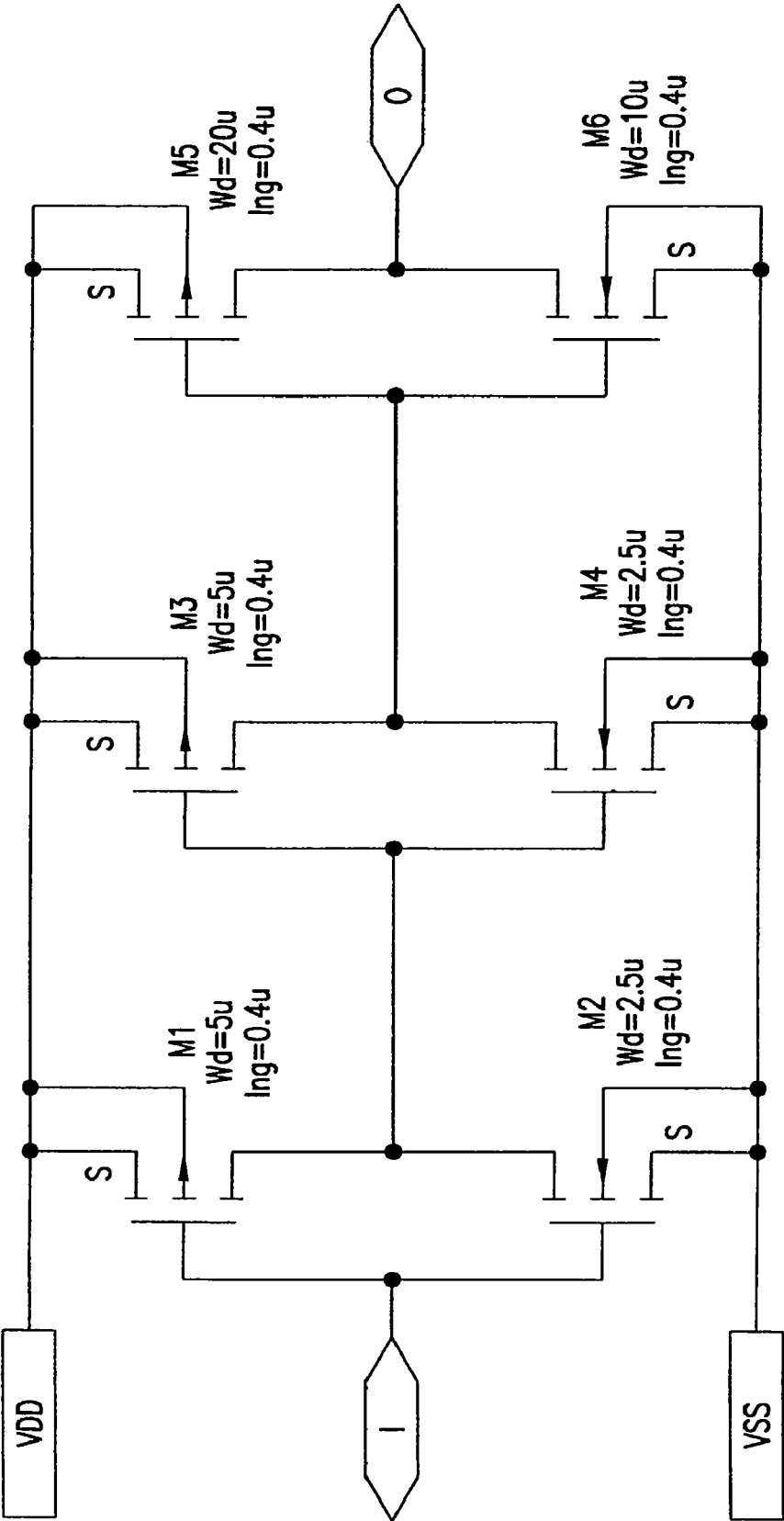


FIG.157

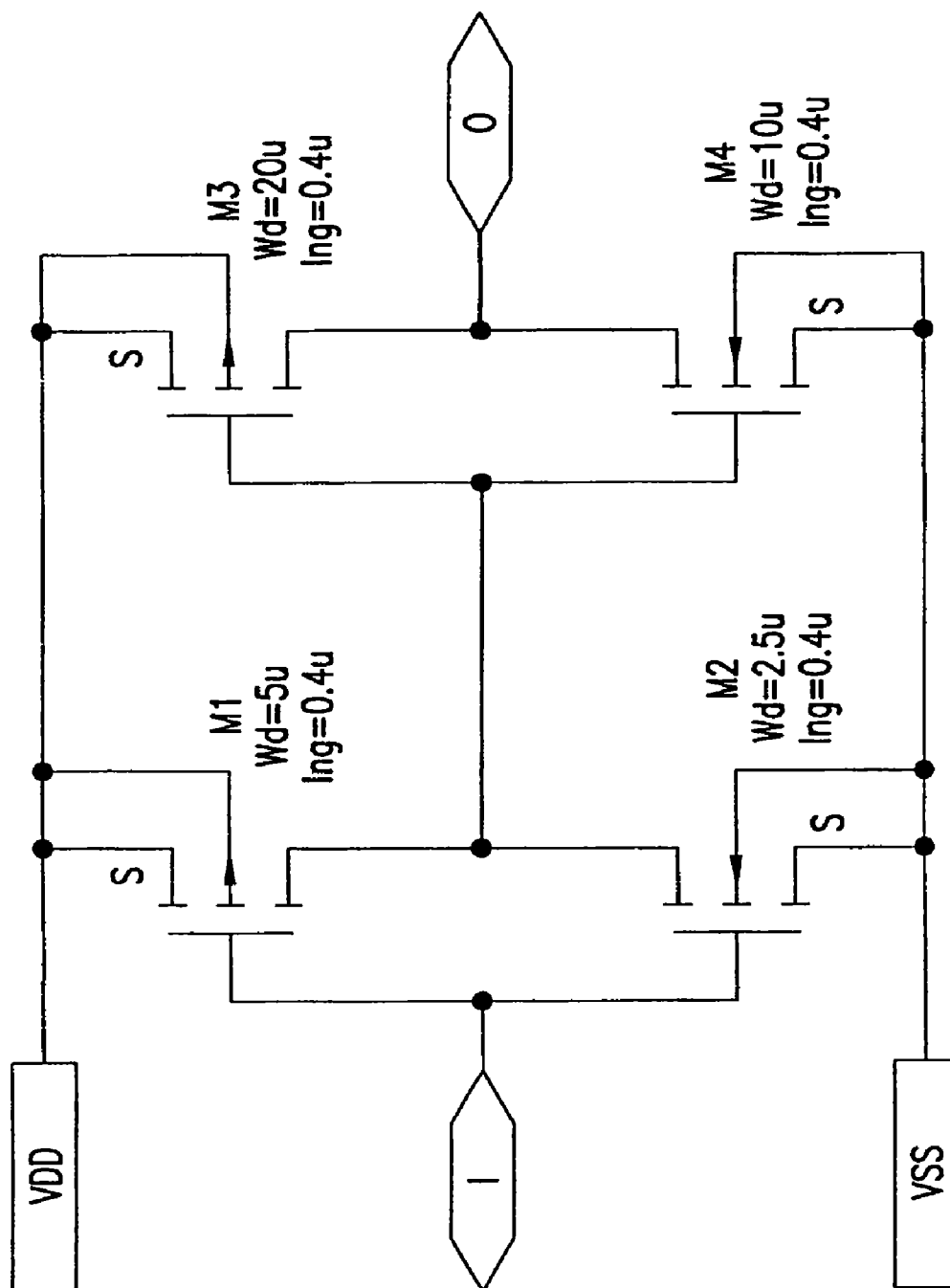


FIG.158

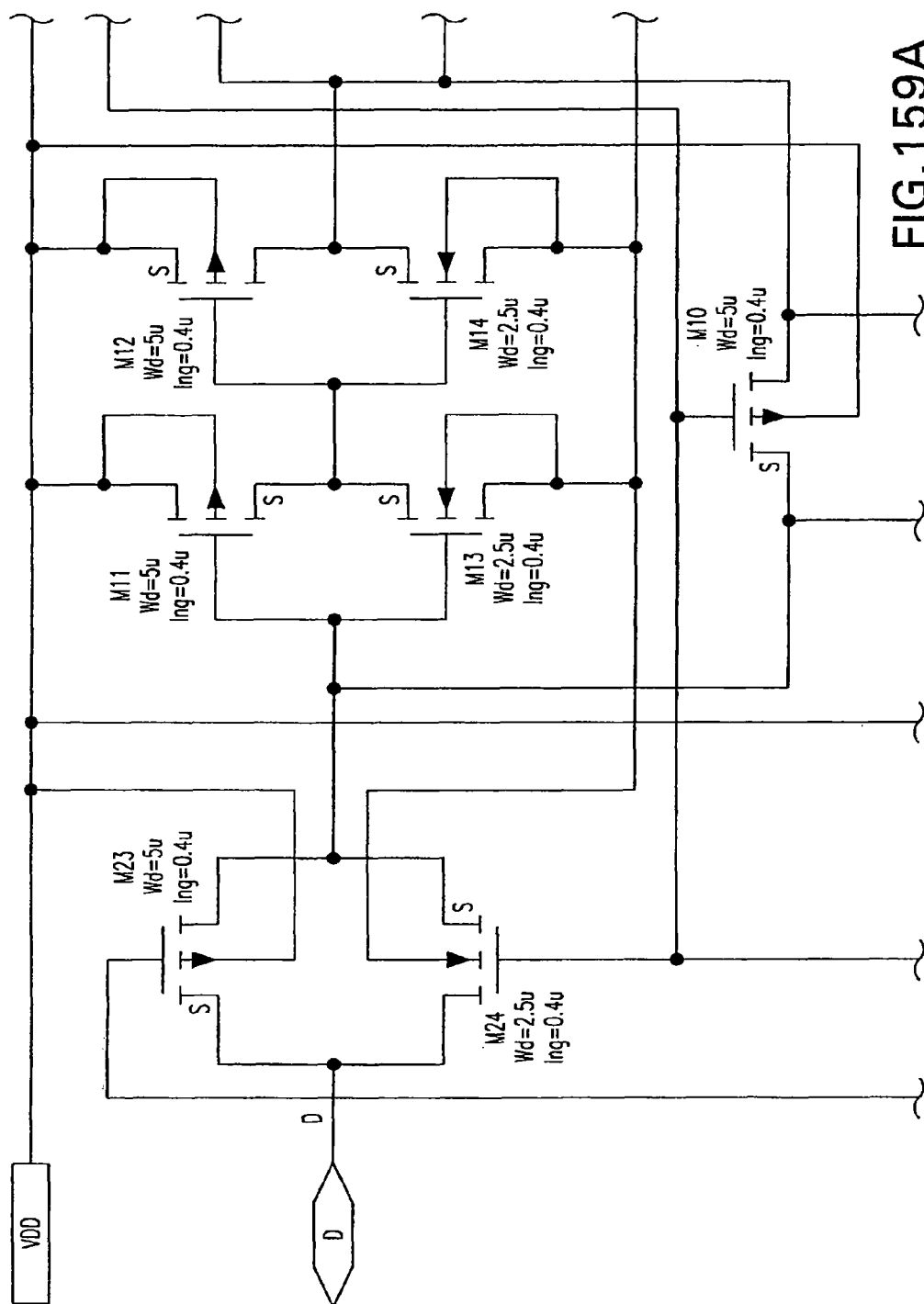


FIG. 159A



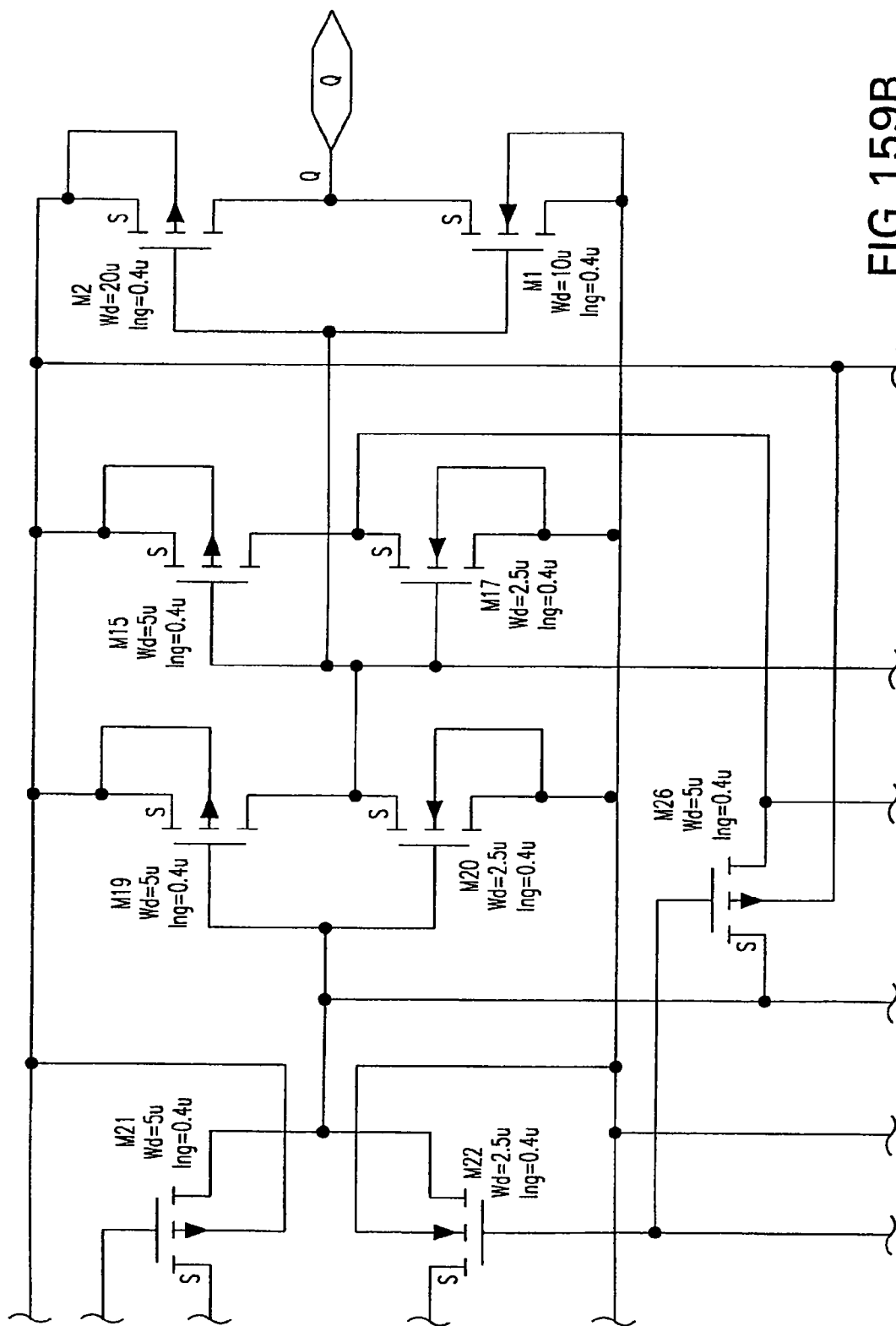
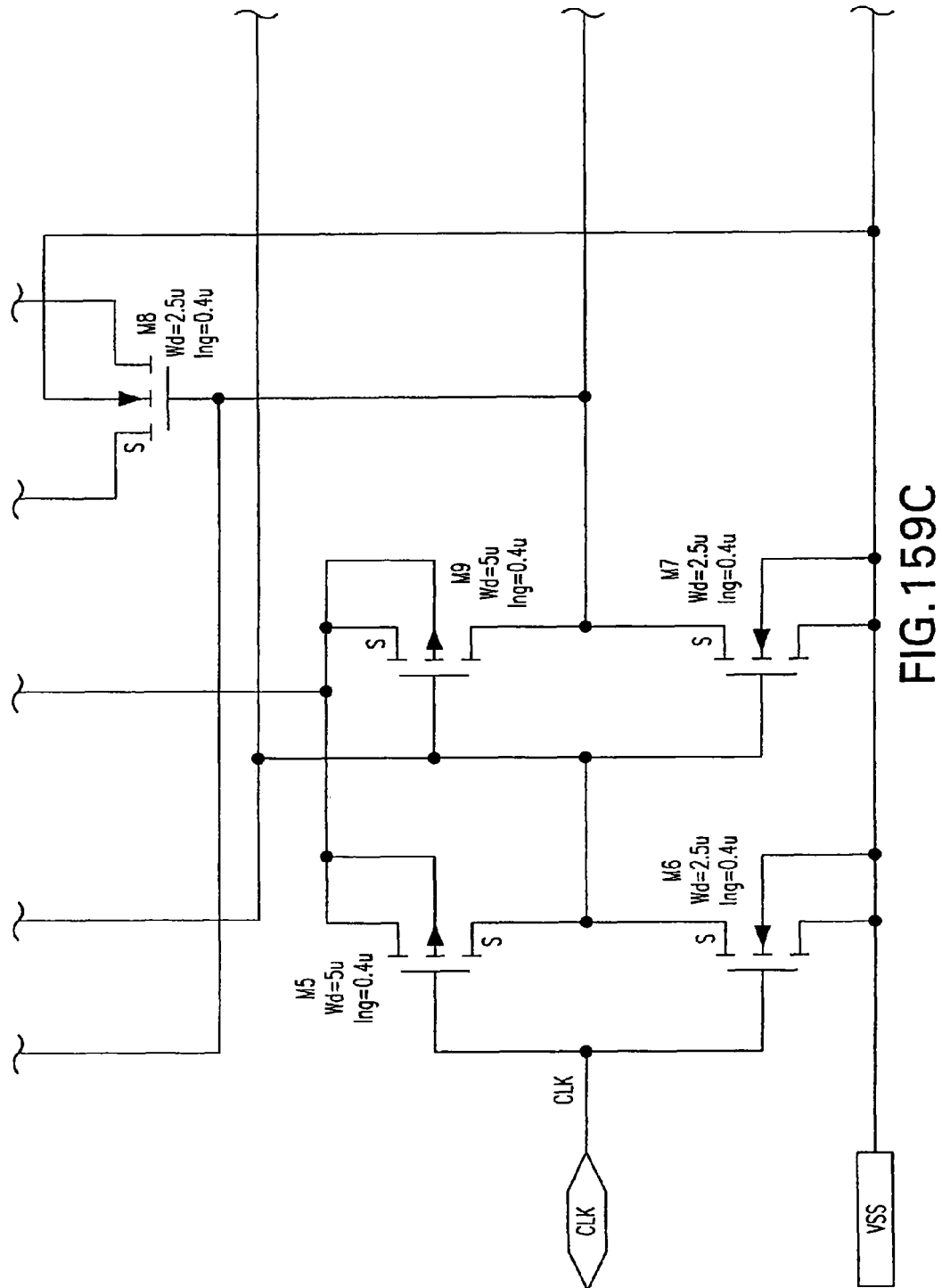


FIG. 159B



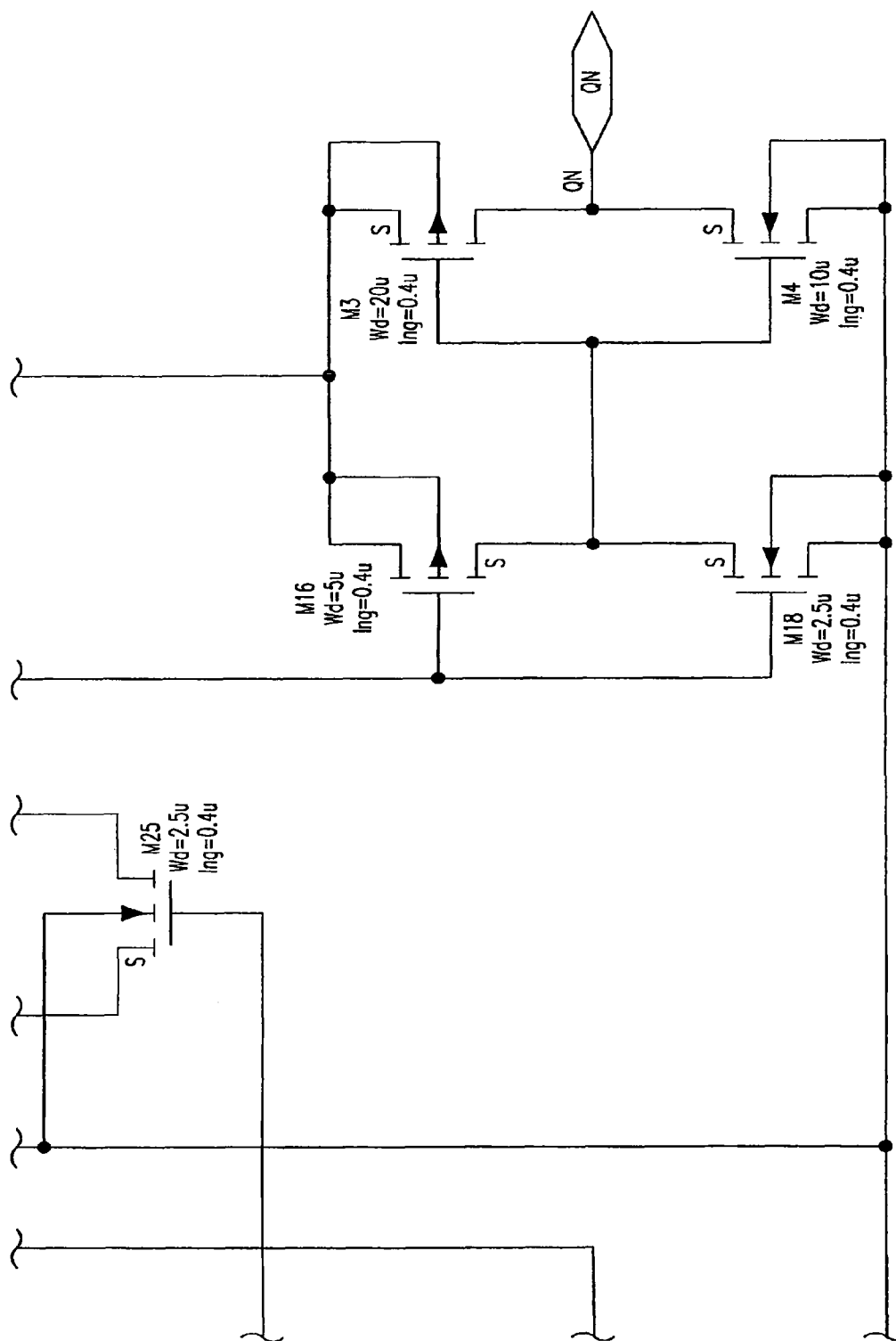


FIG. 159D

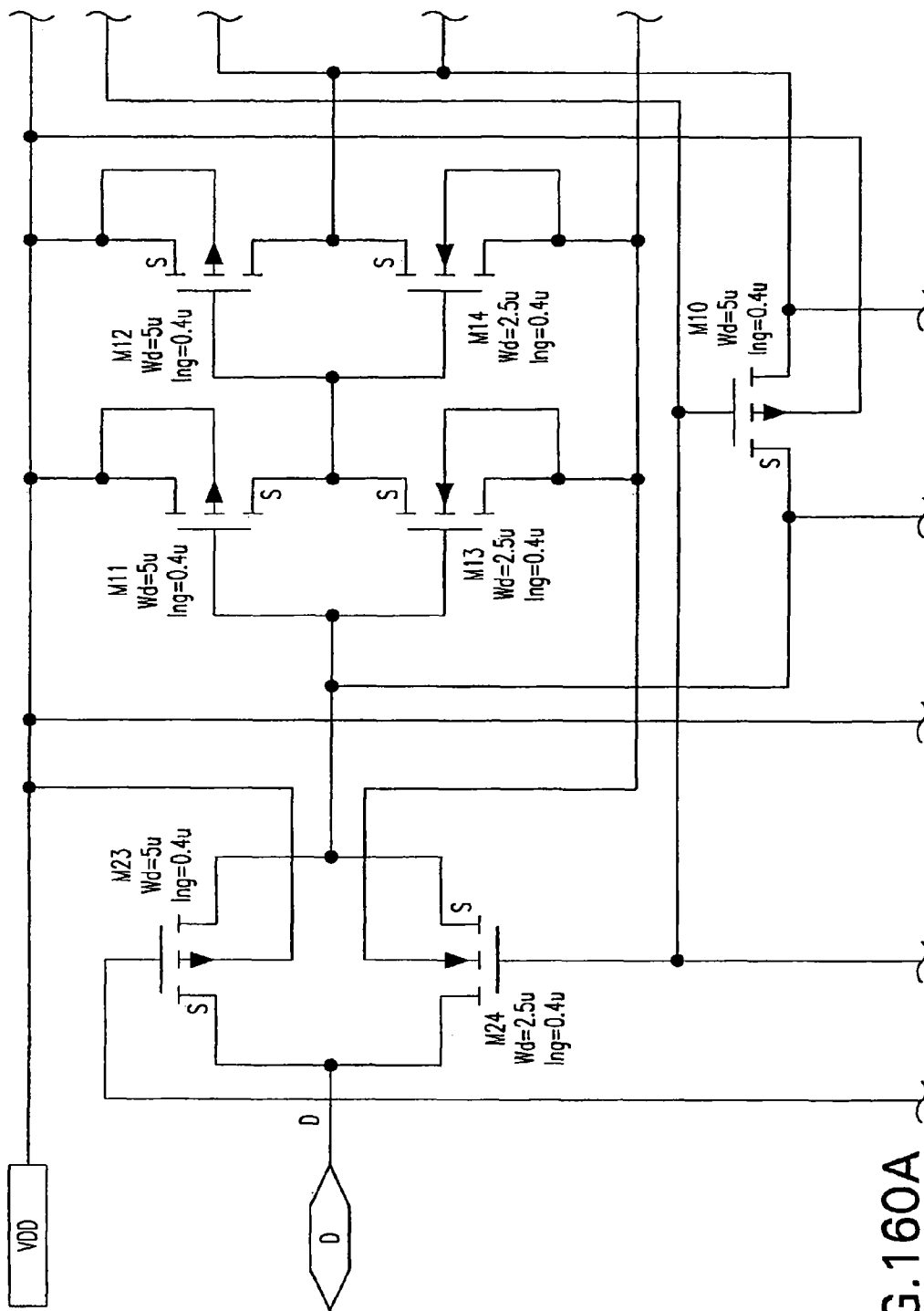


FIG. 160A

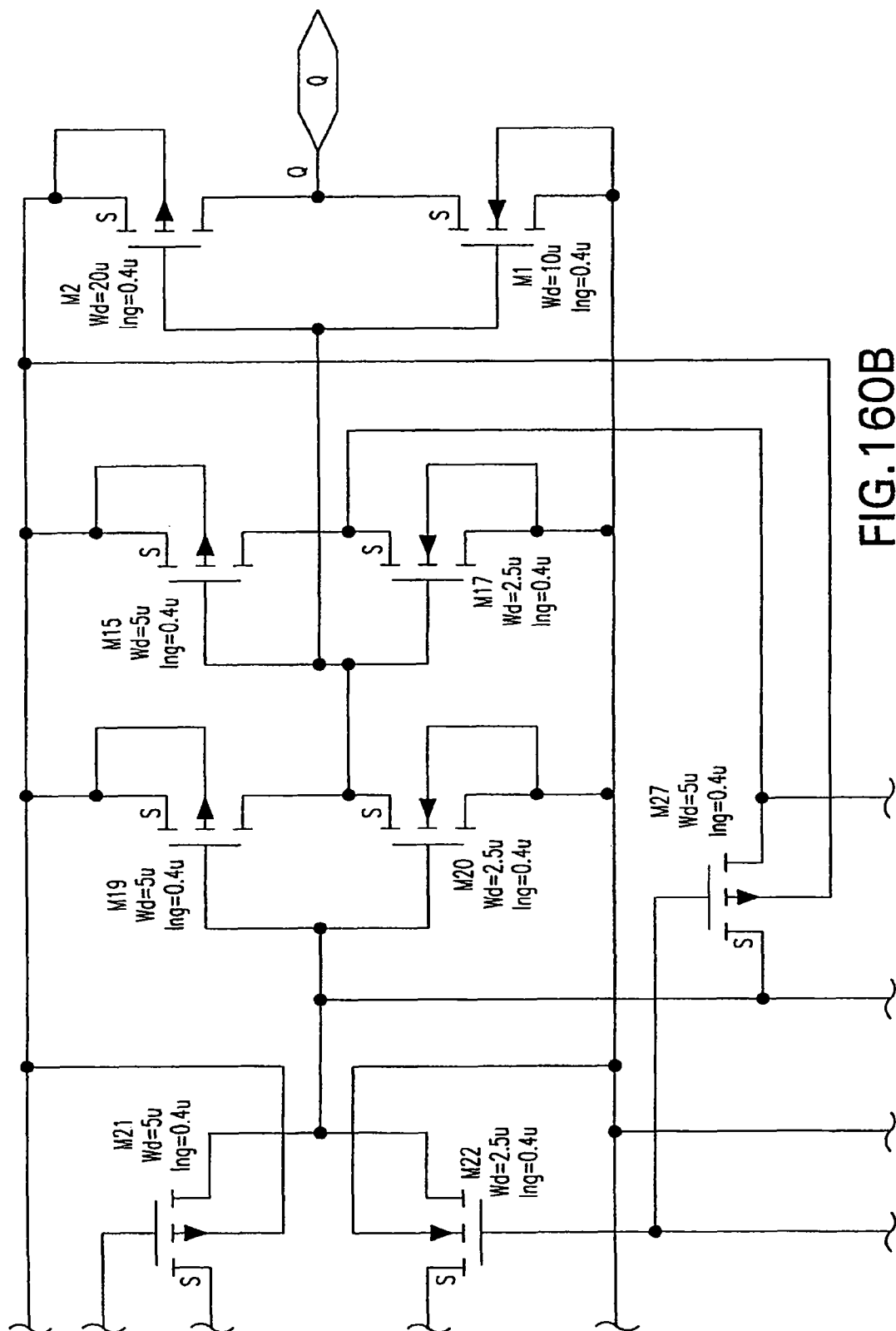
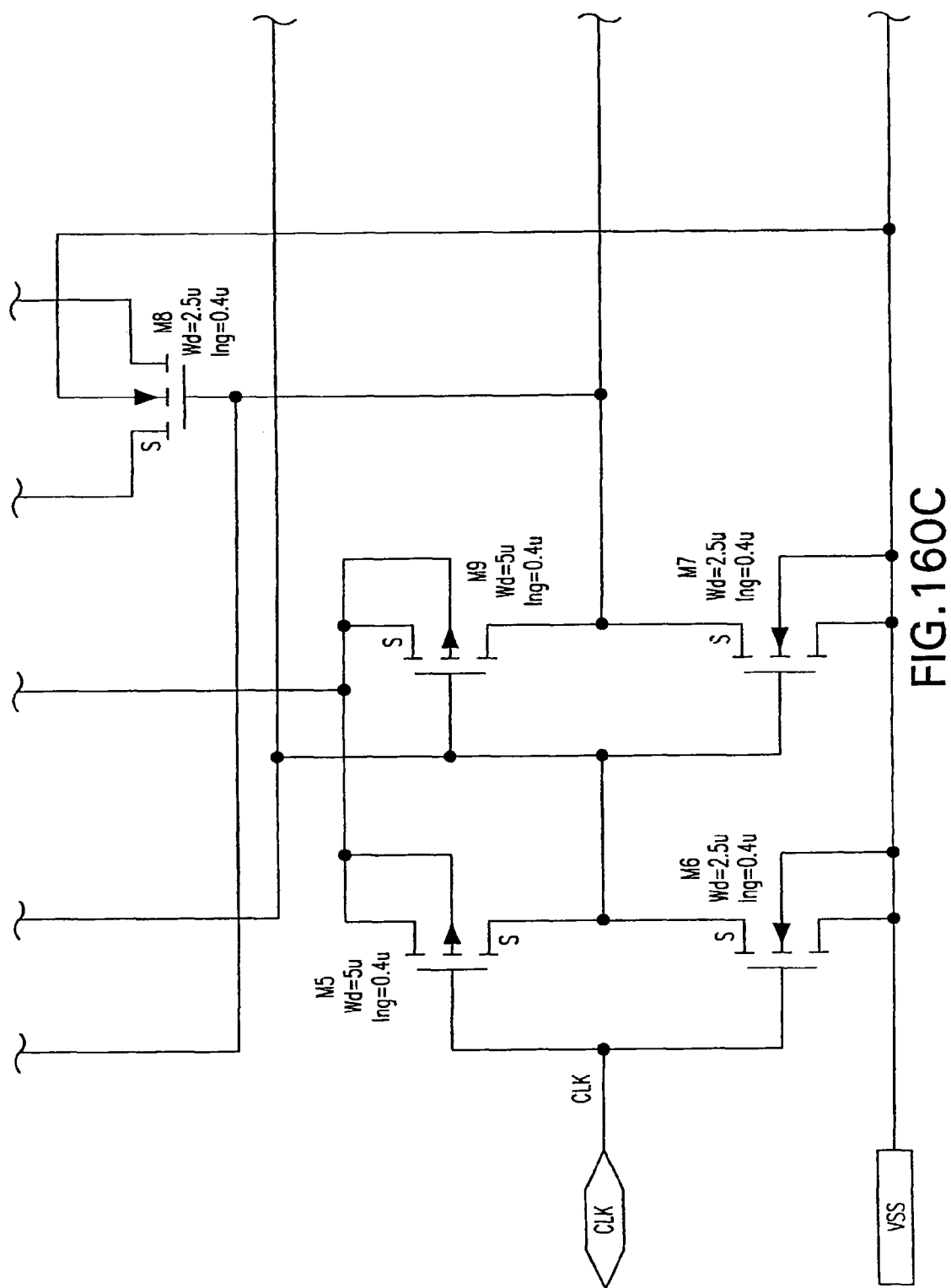


FIG. 160B



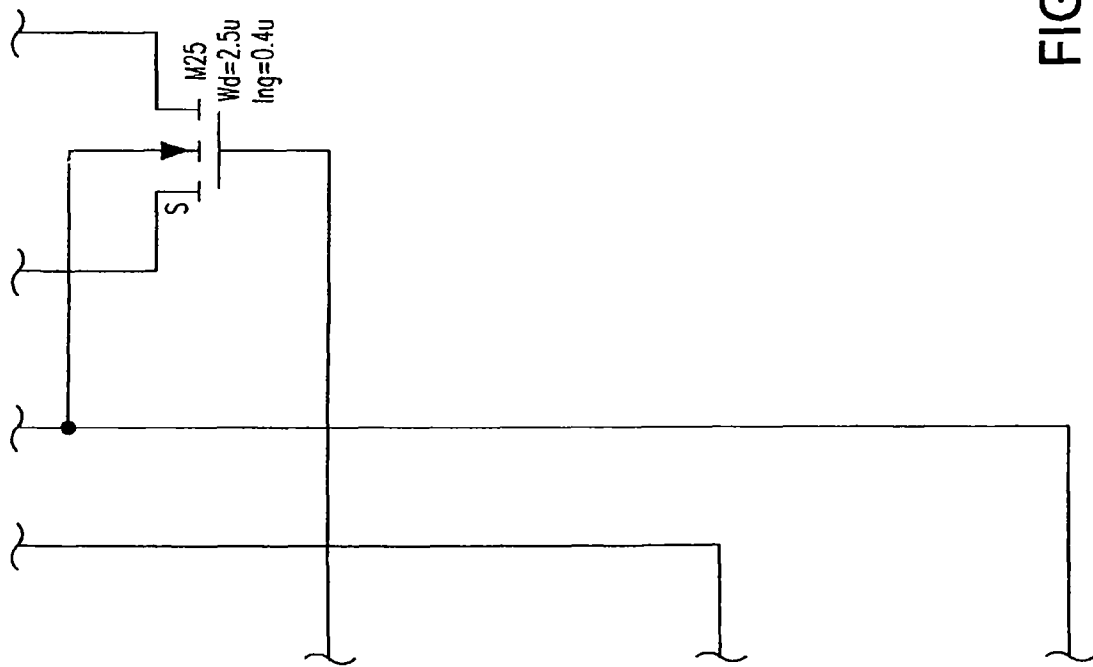


FIG. 160D

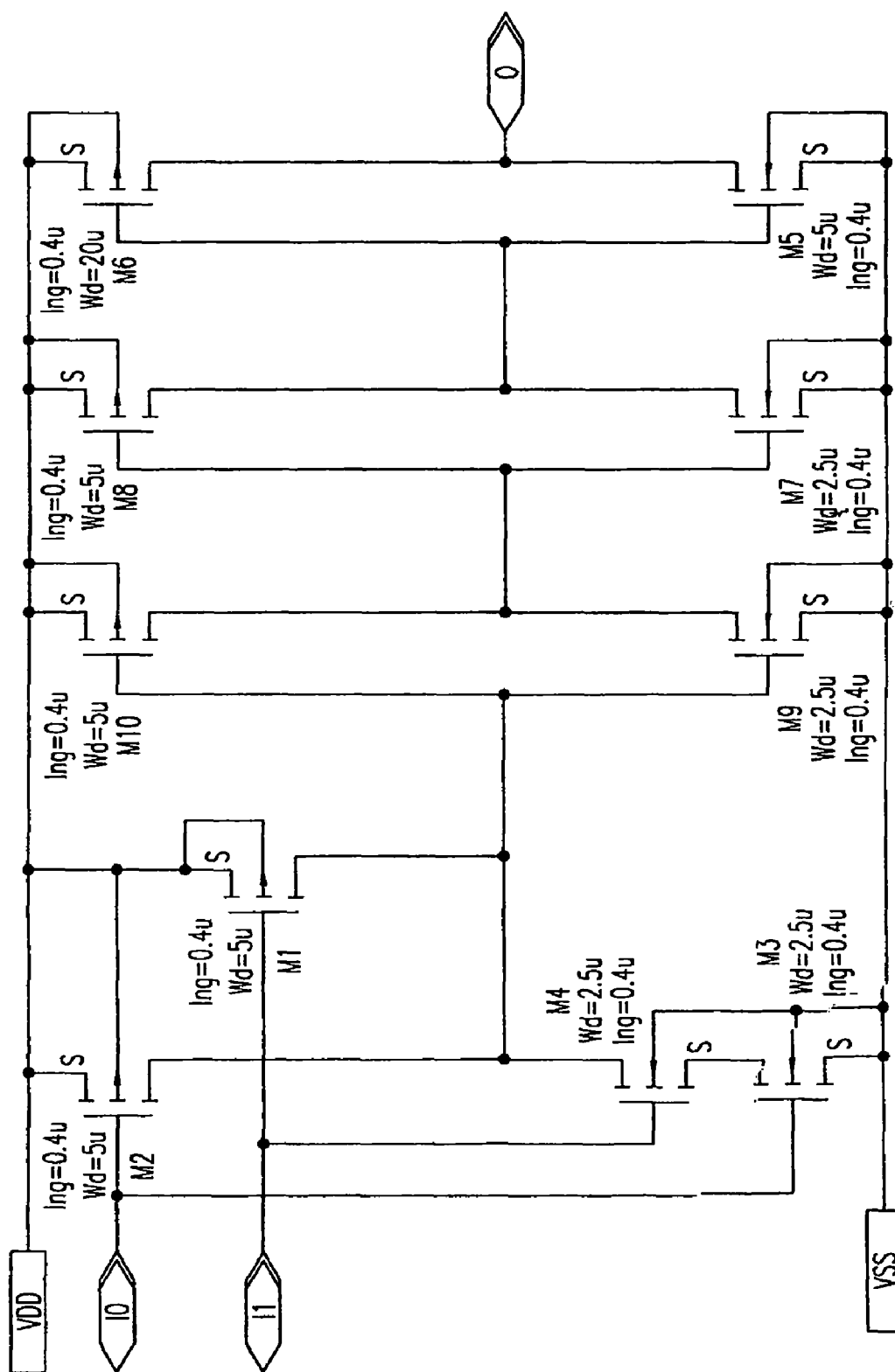


FIG. 161



**WIRELESS LOCAL AREA NETWORK  
(WLAN) USING UNIVERSAL FREQUENCY  
TRANSLATION TECHNOLOGY INCLUDING  
MULTI-PHASE EMBODIMENTS**

This application is a continuation of U.S. patent application Ser. No. 11/041,422, filed Jan. 25, 2005, which is a continuation of U.S. application Ser. No. 09/632,856, filed on Aug. 4, 2000, both of which are incorporated herein by reference in their entireties; U.S. application Ser. No. 09/632,856 claims the benefit of U.S. Provisional Application No. 60/147,129, filed on Aug. 4, 1999; and U.S. application Ser. No. 09/632,856 is a continuation-in-part of U.S. application Ser. No. 09/525,615, filed on Mar. 14, 2000; and U.S. application Ser. No. 09/632,856 is a continuation-in-part of U.S. application Ser. No. 09/526,041, filed on Mar. 14, 2000, all of which are incorporated herein by reference in their entireties; U.S. application Ser. No. 09/525,615 claims priority to the following: U.S. Provisional Application No. 60/177,381, filed on Jan. 24, 2000; U.S. Provisional Application No. 60/171,502, filed Dec. 22, 1999; U.S. Provisional Application No. 60/177,705, filed on Jan. 24, 2000; U.S. Provisional Application No. 60/129,839, filed on Apr. 16, 1999; U.S. Provisional Application No. 60/158,047, filed on Oct. 7, 1999; U.S. Provisional Application No. 60/171,349, filed on Dec. 21, 1999; U.S. Provisional Application No. 60/177,702, filed on Jan. 24, 2000; U.S. Provisional Application No. 60/180,667, filed on Feb. 7, 2000 and U.S. Provisional Application No. 60/171,496, filed on Dec. 22, 1999; all of which are incorporated by reference herein in their entireties.

**CROSS-REFERENCE TO OTHER  
APPLICATIONS**

The following applications of common assignee are related to the present application, and are herein incorporated by reference in their entireties:

“Method and System for Down-Converting Electromagnetic Signals,” Ser. No. 09/176,022, filed Oct. 21, 1998, issued as U.S. Pat. No. 6,061,551 on May 9, 2000.

“Method and System for Down-Converting Electromagnetic Signals Having Optimized Switch Structures,” Ser. No. 09/293,095, filed Apr. 16, 1999.

“Method and System for Down-Converting Electromagnetic Signals Including Resonant Structures for Enhanced Energy Transfer,” Ser. No. 09/293,342, filed Apr. 16, 1999.

“Method and System for Frequency Up-Conversion,” Ser. No. 09/176,154, filed Oct. 21, 1998, issued as U.S. Pat. No. 6,091,940 on Jul. 18, 2000.

“Method and System for Frequency Up-Conversion Having Optimized Switch Structures,” Ser. No. 09/293,097, filed Apr. 16, 1999.

“Method and System for Ensuring Reception of a Communications Signal,” Ser. No. 09/176,415, filed Oct. 21, 1998, issued as U.S. Pat. No. 6,061,555 on May 9, 2000.

“Integrated Frequency Translation And Selectivity,” Ser. No. 09/175,966, filed Oct. 21, 1998, issued as U.S. Pat. No. 6,049,706 on Apr. 11, 2000.

“Integrated Frequency Translation and Selectivity with a Variety of Filter Embodiments,” Ser. No. 09/293,283, filed Apr. 16, 1999.

“Applications of Universal Frequency Translation,” Ser. No. 09/261,129, filed Mar. 3, 1999.

“Method and System for Down-Converting an Electromagnetic Signal, Transforms For Same, and Aperture Relationships,” Ser. No. 09/550,644, filed on Apr. 14, 2000.

“Wireless Local Area Network (WLAN) Technology and Applications Including Techniques of Universal Frequency Translation”, filed on Aug. 4, 2000.

**BACKGROUND OF THE INVENTION**

**1. Field of the Invention**

The present invention is generally related to wireless local area networks (WLANs), and more particularly, to WLANs that utilize universal frequency translation technology for frequency translation, and applications of same.

**2. Related Art**

Wireless LANs exist for receiving and transmitting information to/from mobile terminals using electromagnetic (EM) signals. Conventional wireless communications circuitry is complex and has a large number of circuit parts. This complexity and high parts count increases overall cost. Additionally, higher part counts result in higher power consumption, which is undesirable, particularly in battery powered wireless units. Additionally, various communication components exist for performing frequency down-conversion, frequency up-conversion, and filtering. Also, schemes exist for signal reception in the face of potential jamming signals.

**BRIEF SUMMARY OF THE INVENTION**

The present invention is directed to a wireless local area network (WLAN) that includes one or more WLAN devices (also called stations, terminals, access points, client devices, or infrastructure devices) for effecting wireless communications over the WLAN. The WLAN device includes at least an antenna, a receiver, and a transmitter for effecting wireless communications over the WLAN. Additionally, the WLAN device may also include a LNA/PA module, a control signal generator, a demodulation/modulation facilitation module, and a media access control (MAC) interface. The WLAN receiver includes at least one universal frequency translation module that frequency down-converts a received electromagnetic (EM) signal. In embodiments, the UFT based receiver is configured in a multi-phase embodiment to reduce or eliminate re-radiation that is caused by DC offset. The WLAN transmitter includes at least one universal frequency translation module that frequency up-converts a baseband signal in preparation for transmission over the WLAN. In embodiments, the UFT based transmitter is configured in a differential and/or multi-phase embodiment to reduce carrier insertion and spectral growth in the transmitted signal.

WLANs exhibit multiple advantages by using UFT modules for frequency translation. These advantages include, but are not limited to: lower power consumption, longer battery life, fewer parts, lower cost, less tuning, and more effective signal transmission and reception. These advantages are possible because the UFT module enables direct frequency conversion in an efficient manner with minimal signal distortion. The structure and operation of embodiments of the UFT module, and various applications of the same are described in detail in the following sections.

Further features and advantages of the invention, as well as the structure and operation of various embodiments of the invention, are described in detail below with reference to the accompanying drawings. The drawing in which an element first appears is typically indicated by the leftmost character(s) and/or digit(s) in the corresponding reference number.

**BRIEF DESCRIPTION OF THE FIGURES**

The present invention will be described with reference to the accompanying drawings, wherein:

FIG. 1A is a block diagram of a universal frequency translation (UFT) module according to an embodiment of the invention;

FIG. 1B is a more detailed diagram of a universal frequency translation (UFT) module according to an embodiment of the invention;

FIG. 1C illustrates a UFT module used in a universal frequency down-conversion (UFD) module according to an embodiment of the invention;

FIG. 1D illustrates a UFT module used in a universal frequency up-conversion (UFU) module according to an embodiment of the invention;

FIG. 2A-2B illustrate block diagrams of universal frequency translation (UFT) modules according to an embodiment of the invention;

FIG. 3 is a block diagram of a universal frequency up-conversion (UFU) module according to an embodiment of the invention;

FIG. 4 is a more detailed diagram of a universal frequency up-conversion (UFU) module according to an embodiment of the invention;

FIG. 5 is a block diagram of a universal frequency up-conversion (UFU) module according to an alternative embodiment of the invention;

FIGS. 6A-6I illustrate example waveforms used to describe the operation of the UFU module;

FIG. 7 illustrates a UFT module used in a receiver according to an embodiment of the invention;

FIG. 8 illustrates a UFT module used in a transmitter according to an embodiment of the invention;

FIG. 9 illustrates an environment comprising a transmitter and a receiver, each of which may be implemented using a UFT module of the invention;

FIG. 10 illustrates a transceiver according to an embodiment of the invention;

FIG. 11 illustrates a transceiver according to an alternative embodiment of the invention;

FIG. 12 illustrates an environment comprising a transmitter and a receiver, each of which may be implemented using enhanced signal reception (ESR) components of the invention;

FIG. 13 illustrates a UFT module used in a unified down-conversion and filtering (UDF) module according to an embodiment of the invention;

FIG. 14 illustrates an example receiver implemented using a UDF module according to an embodiment of the invention;

FIGS. 15A-15F illustrate example applications of the UDF module according to embodiments of the invention;

FIG. 16 illustrates an environment comprising a transmitter and a receiver, each of which may be implemented using enhanced signal reception (ESR) components of the invention, wherein the receiver may be further implemented using one or more UFD modules of the invention;

FIG. 17 illustrates a unified down-converting and filtering (UDF) module according to an embodiment of the invention;

FIG. 18 is a table of example values at nodes in the UDF module of FIG. 19;

FIG. 19 is a detailed diagram of an example UDF module according to an embodiment of the invention;

FIGS. 20A and 20A-1 are example aliasing modules according to embodiments of the invention;

FIGS. 20B-20F are example waveforms used to describe the operation of the aliasing modules of FIGS. 20A and 20A-1;

FIG. 21 illustrates an enhanced signal reception system according to an embodiment of the invention;

FIGS. 22A-22F are example waveforms used to describe the system of FIG. 21;

FIG. 23A illustrates an example transmitter in an enhanced signal reception system according to an embodiment of the invention;

FIGS. 23B and 23C are example waveforms used to further describe the enhanced signal reception system according to an embodiment of the invention;

FIG. 23D illustrates another example transmitter in an enhanced signal reception system according to an embodiment of the invention;

FIGS. 23E and 23F are example waveforms used to further describe the enhanced signal reception system according to an embodiment of the invention;

FIG. 24A illustrates an example receiver in an enhanced signal reception system according to an embodiment of the invention;

FIGS. 24B-24J are example waveforms used to further describe the enhanced signal reception system according to an embodiment of the invention;

FIG. 25 illustrates a block diagram of an example computer network;

FIG. 26 illustrates a block diagram of an example computer network;

FIG. 27 illustrates a block diagram of an example wireless interface;

FIG. 28 illustrates an example heterodyne implementation of the wireless interface illustrated in FIG. 27;

FIG. 29 illustrates an example in-phase/quadrature-phase (UQ) heterodyne implementation of the interface illustrated in FIG. 27;

FIG. 30 illustrates an example high level block diagram of the interface illustrated in FIG. 27, in accordance with the present invention;

FIG. 31 illustrates a example block diagram of the interface illustrated in FIG. 29, in accordance with the invention;

FIG. 32 illustrates an example I/Q implementation of the interface illustrated in FIG. 31;

FIGS. 33-38 illustrate example environments encompassed by the invention;

FIG. 39 illustrates a block diagram of a WLAN interface according to an embodiment of the invention;

FIG. 40 illustrates a WLAN receiver according to an embodiment of the invention;

FIG. 41 illustrates a WLAN transmitter according to an embodiment of the invention;

FIGS. 42-44 are example implementations of a WLAN interface;

FIGS. 45, 46A-C relate to an example MAC interface for an example WLAN interface embodiment;

FIGS. 47, 48, 49A-C relate to an example demodulator/modulator facilitation module for an example WLAN interface embodiment;

FIGS. 50, 51, 52A, 52B, and 52C relate to an example alternate demodulator/modulator facilitation module for an example WLAN interface embodiment;

FIGS. 53 and 54 relate to an example receiver for an example WLAN interface embodiment;

FIGS. 55, 56A, and 56B relate to an example synthesizer for an example WLAN interface embodiment;

FIGS. 57, 58, 59, 60, 61A, and 61B relate to an example transmitter for an example WLAN interface embodiment;

FIGS. 62 and 63 relate to an example motherboard for an example WLAN interface embodiment;

FIGS. 64-66 relate to example LNAs for an example WLAN interface embodiment;

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FIGS. 67A-B illustrate IQ receivers having UFT modules in a series and shunt configurations, according to embodiments of the invention;

FIGS. 68A-B illustrate IQ receivers having UFT modules with delayed control signals for quadrature implementation, according to embodiments of the present invention;

FIGS. 69A-B illustrate IQ receivers having FET implementations, according to embodiments of the invention;

FIG. 70A illustrates an IQ receiver having shunt UFT modules according to embodiments of the invention;

FIG. 70B illustrates control signal generator embodiments for receiver 7000 according to embodiments of the invention;

FIGS. 70C-D illustrate various control signal waveforms according to embodiments of the invention;

FIG. 70E illustrates an example IQ modulation receiver embodiment according to embodiments of the invention;

FIGS. 70E-P illustrate example waveforms that are representative of the IQ receiver in FIG. 70E;

FIGS. 70Q-R illustrate single channel receiver embodiments according to embodiments of the invention;

FIG. 70S illustrates a FET configuration of an IQ receiver embodiment according to embodiments of the invention;

FIG. 71A illustrate a balanced transmitter 7102, according to an embodiment of the present invention;

FIGS. 71B-C illustrate example waveforms that are associated with the balanced transmitter 7102, according to an embodiment of the present invention;

FIG. 71D illustrates example FET configurations of the balanced transmitter 7102, according to embodiments of the present invention;

FIGS. 72A-I illustrate various example timing diagrams that are associated with the transmitter 7102, according to embodiments of the present invention;

FIG. 72J illustrates an example frequency spectrum that is associated with a modulator 7104, according to embodiments of the present invention;

FIG. 73A illustrate a transmitter 7302 that is configured for carrier insertion, according to embodiments of the present invention;

FIG. 73B illustrates example signals associated with the transmitter 7302, according to embodiments of the invention;

FIG. 74 illustrates an IQ balanced transmitter 7420, according to embodiments of the present invention;

FIGS. 75A-C illustrate various example signal diagrams associated with the balanced transmitter 7420 in FIG. 74;

FIG. 76A illustrates an IQ balanced transmitter 7608 according to embodiments of the invention;

FIG. 76B illustrates an IQ balanced modulator 7618 according to embodiments of the invention;

FIG. 77 illustrates an IQ balanced modulator 7702 configured for carrier insertion according to embodiments of the invention;

FIG. 78 illustrates an IQ balanced modulator 7802 configured for carrier insertion according to embodiments of the invention;

FIG. 79A illustrate a transmitter 7900, according to embodiments of the present invention;

FIGS. 79B-C illustrate various frequency spectrums that are associated with the transmitter 7900;

FIG. 79D illustrates a FET configuration for the transmitter 7900, according to embodiments of the present invention;

FIG. 80 illustrates an IQ transmitter 8000, according to embodiments of the present invention;

FIGS. 81A-C illustrate various frequency spectrums that are associated with the IQ transmitter 8000, according to embodiments of the present invention;

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FIG. 82 illustrates an IQ transmitter 8200, according to embodiments of the present invention;

FIG. 83 illustrates an IQ transmitter 8300, according to embodiments of the invention;

FIG. 84 illustrates a flowchart 8400 that is associated with the transmitter 7102 in the FIG. 71A, according to embodiments of the invention;

FIG. 85 illustrates a flowchart 8500 that further defines the flowchart 8400 in the FIG. 84, and is associated with the transmitter 7102 according to embodiments of the invention;

FIG. 86 illustrates a flowchart 8600 that is associated with the transmitter 7900 and further defines the flowchart 8400 in the FIG. 84, according to embodiments of the invention;

FIG. 87 illustrates a flowchart 8700, that is associated with the transmitter 7420 in the FIG. 74, according to embodiments of the invention;

FIG. 88 illustrates a flowchart 8800 that is associated with the transmitter 8000, according to embodiments of the invention;

FIG. 89A illustrate a pulse generator according to embodiments of the invention;

FIGS. 89B-C illustrate various example signal diagrams associated with the pulse generator in FIG. 89A, according to embodiments of the invention;

FIG. 89D-E illustrate various example pulse generators according to embodiments of the present invention;

FIGS. 90A-D illustrates various implementation circuits for the modulator 7410, according to embodiments of the present invention;

FIG. 91 illustrates an IQ transceiver 9100 according to embodiments of the present invention;

FIG. 92 illustrates direct sequence spread spectrum according to embodiments of the present invention;

FIG. 93 illustrates the LNA/PA module 3904 according to embodiments of the present invention; and

FIG. 94 illustrates a WLAN device 9400, according to embodiments of the invention of the present invention.

FIGS. 95A-C, and FIGS. 96-161 illustrate schematics for an integrated circuit implementation example of the present invention.

## DETAILED DESCRIPTION OF THE PREFERRED EMBODIMENTS

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## 1. UNIVERSAL FREQUENCY TRANSLATION

The present invention is related to frequency translation, and applications of same. Such applications include, but are not limited to, frequency down-conversion, frequency up-conversion, enhanced signal reception, unified down-conversion and filtering, and combinations and applications of same.

FIG. 1A illustrates a universal frequency translation (UFT) module **102** according to embodiments of the invention. (The UFT module is also sometimes called a universal frequency translator, or a universal translator.)

As indicated by the example of FIG. 1A, some embodiments of the UFT module **102** include three ports (nodes), designated in FIG. 1A as Port **1**, Port **2**, and Port **3**. Other UFT embodiments include other than three ports.

Generally, the UFT module **102** (perhaps in combination with other components) operates to generate an output signal from an input signal, where the frequency of the output signal differs from the frequency of the input signal. In other words, the UFT module **102** (and perhaps other components) operates to generate the output signal from the input signal by translating the frequency (and perhaps other characteristics) of the input signal to the frequency (and perhaps other characteristics) of the output signal.

An example embodiment of the UFT module **103** is generally illustrated in FIG. 1B. Generally, the UFT module **103** includes a switch **106** controlled by a control signal **108**. The switch **106** is said to be a controlled switch.

As noted above, some UFT embodiments include other than three ports. For example, and without limitation, FIG. 2 illustrates an example UFT module **202**. The example UFT module **202** includes a diode **204** having two ports, designated as Port **1** and Port **2/3**. This embodiment does not include a third port, as indicated by the dotted line around the "Port **3**" label.

The UFT module is a very powerful and flexible device. Its flexibility is illustrated, in part, by the wide range of applications in which it can be used. Its power is illustrated, in part, by the usefulness and performance of such applications.

For example, a UFT module **115** can be used in a universal frequency down-conversion (UFD) module **114**, an example of which is shown in FIG. 1C. In this capacity, the UFT module **115** frequency down-converts an input signal to an output signal.

As another example, as shown in FIG. 1D, a UFT module **117** can be used in a universal frequency up-conversion (UFU) module **116**. In this capacity, the UFT module **117** frequency up-converts an input signal to an output signal.

These and other applications of the UFT module are described below. Additional applications of the UFT module will be apparent to persons skilled in the relevant art(s) based on the teachings contained herein. In some applications, the UFT module is a required component. In other applications, the UFT module is an optional component.

## 2. FREQUENCY DOWN-CONVERSION

The present invention is directed to systems and methods of universal frequency down-conversion, and applications of same.

In particular, the following discussion describes down-converting using a Universal Frequency Translation Module.

The down-conversion of an EM signal by aliasing the EM signal at an aliasing rate is fully described in co-pending U.S. patent application entitled "Method and System for Down-Converting Electromagnetic Signals," Ser. No. 09/176,022, filed Oct. 21, 1998, issued as U.S. Pat. No. 6,061,551 on May 9, 2000, the full disclosure of which is incorporated herein by reference. A relevant portion of the above mentioned patent application is summarized below to describe down-converting an input signal to produce a down-converted signal that exists at a lower frequency or a baseband signal.

FIG. 20A illustrates an aliasing module **2000** (also called a universal frequency down-conversion module) for down-conversion using a universal frequency translation (UFT) module **2002** which down-converts an EM input signal **2004**. In particular embodiments, aliasing module **2000** includes a switch **2008** and a capacitor **2010**. The electronic alignment of the circuit components is flexible. That is, in one implementation, the switch **2008** is in series with input signal **2004** and capacitor **2010** is shunted to ground (although it may be other than ground in configurations such as differential mode). In a second implementation (see FIG. 20A-1), the capacitor **2010** is in series with the input signal **2004** and the switch **2008** is shunted to ground (although it may be other than ground in configurations such as differential mode). Aliasing module **2000** with UFT module **2002** can be easily tailored to down-convert a wide variety of electromagnetic signals using aliasing frequencies that are well below the frequencies of the EM input signal **2004**.

In one implementation, aliasing module **2000** down-converts the input signal **2004** to an intermediate frequency (IF) signal. In another implementation, the aliasing module **2000** down-converts the input signal **2004** to a demodulated baseband signal. In yet another implementation, the input signal **2004** is a frequency modulated (FM) signal, and the aliasing module **2000** down-converts it to a non-FM signal, such as a phase modulated (PM) signal or an amplitude modulated (AM) signal. Each of the above implementations is described below.

In an embodiment, the control signal **2006** includes a train of pulses that repeat at an aliasing rate that is equal to, or less than, twice the frequency of the input signal **2004**. In this embodiment, the control signal **2006** is referred to herein as an aliasing signal because it is below the Nyquist rate for the

frequency of the input signal **2004**. Preferably, the frequency of control signal **2006** is much less than the input signal **2004**.

A train of pulses **2018** as shown in FIG. **20D** controls the switch **2008** to alias the input signal **2004** with the control signal **2006** to generate a down-converted output signal **2012**. More specifically, in an embodiment, switch **2008** closes on a first edge of each pulse **2020** of FIG. **20D** and opens on a second edge of each pulse. When the switch **2008** is closed, the input signal **2004** is coupled to the capacitor **2010**, and charge is transferred from the input signal to the capacitor **2010**. The charge stored during successive pulses forms down-converted output signal **2012**.

Exemplary waveforms are shown in FIGS. **20B-20F**.

FIG. **20B** illustrates an analog amplitude modulated (AM) carrier signal **2014** that is an example of input signal **2004**. For illustrative purposes, in FIG. **20C**, an analog AM carrier signal portion **2016** illustrates a portion of the analog AM carrier signal **2014** on an expanded time scale. The analog AM carrier signal portion **2016** illustrates the analog AM carrier signal **2014** from time  $t_0$  to time  $t_1$ .

FIG. **20D** illustrates an exemplary aliasing signal **2018** that is an example of control signal **2006**. Aliasing signal **2018** is on approximately the same time scale as the analog AM carrier signal portion **2016**. In the example shown in FIG. **20D**, the aliasing signal **2018** includes a train of pulses **2020** having negligible apertures that tend towards zero (the invention is not limited to this embodiment, as discussed below). The pulse aperture may also be referred to as the pulse width as will be understood by those skilled in the art(s). The pulses **2020** repeat at an aliasing rate, or pulse repetition rate of aliasing signal **2018**. The aliasing rate is determined as described below, and further described in co-pending U.S. patent application entitled "Method and System for Down-converting Electromagnetic Signals," application Ser. No. 09/176,022, issued as U.S. Pat. No. 6,061,551 on May 9, 2000.

As noted above, the train of pulses **2020** (i.e., control signal **2006**) control the switch **2008** to alias the analog AM carrier signal **2016** (i.e., input signal **2004**) at the aliasing rate of the aliasing signal **2018**. Specifically, in this embodiment, the switch **2008** closes on a first edge of each pulse and opens on a second edge of each pulse. When the switch **2008** is closed, input signal **2004** is coupled to the capacitor **2010**, and charge is transferred from the input signal **2004** to the capacitor **2010**. The charge transferred during a pulse is referred to herein as an under-sample. Exemplary under-samples **2022** form down-converted signal portion **2024** (FIG. **20E**) that corresponds to the analog AM carrier signal portion **2016** (FIG. **20C**) and the train of pulses **2020** (FIG. **20D**). The charge stored during successive under-samples of AM carrier signal **2014** form the down-converted signal **2024** (FIG. **20E**) that is an example of down-converted output signal **2012** (FIG. **20A**). In FIG. **20F**, a demodulated baseband signal **2026** represents the demodulated baseband signal **2024** after filtering on a compressed time scale. As illustrated, down-converted signal **2026** has substantially the same "amplitude envelope" as AM carrier signal **2014**. Therefore, FIGS. **20B-20F** illustrate down-conversion of AM carrier signal **2014**.

The waveforms shown in FIGS. **20B-20F** are discussed herein for illustrative purposes only, and are not limiting. Additional exemplary time domain and frequency domain drawings, and exemplary methods and systems of the invention relating thereto, are disclosed in co-pending U.S. patent application entitled "Method and System for Down-converting Electromagnetic Signals," application Ser. No. 09/176,022, issued as U.S. Pat. No. 6,061,551 on May 9, 2000.

The aliasing rate of control signal **2006** determines whether the input signal **2004** is down-converted to an IF signal, down-converted to a demodulated baseband signal, or down-converted from an FM signal to a PM or an AM signal. Generally, relationships between the input signal **2004**, the aliasing rate of the control signal **2006**, and the down-converted output signal **2012** are illustrated below:

$$(\text{Freq. of input signal } 2004) = n \cdot (\text{Freq. of control signal } 2006) \pm (\text{Freq. of down-converted output signal } 2012)$$

For the examples contained herein, only the "+" condition will be discussed. The value of  $n$  represents a harmonic or sub-harmonic of input signal **2004** (e.g.,  $n=0.5, 1, 2, 3, \dots$ ).

When the aliasing rate of control signal **2006** is off-set from the frequency of input signal **2004**, or off-set from a harmonic or sub-harmonic thereof, input signal **2004** is down-converted to an IF signal. This is because the under-sampling pulses occur at different phases of subsequent cycles of input signal **2004**. As a result, the under-samples form a lower frequency oscillating pattern. If the input signal **2004** includes lower frequency changes, such as amplitude, frequency, phase, etc., or any combination thereof, the charge stored during associated under-samples reflects the lower frequency changes, resulting in similar changes on the down-converted IF signal. For example, to down-convert a 901 MHz input signal to a 1 MHz IF signal, the frequency of the control signal **2006** would be calculated as follows:

$$(\text{Freq}_{\text{input}} - \text{Freq}_{\text{IF}}) / n = \text{Freq}_{\text{control}}$$

$$(901 \text{ MHz} - 1 \text{ MHz}) / n = 900 / n$$

For  $n=0.5, 1, 2, 3, 4$ , etc., the frequency of the control signal **2006** would be substantially equal to 1.8 GHz, 900 MHz, 450 MHz, 300 MHz, 225 MHz, etc.

Exemplary time domain and frequency domain drawings, illustrating down-conversion of analog and digital AM, PM and FM signals to IF signals, and exemplary methods and systems thereof, are disclosed in co-pending U.S. patent application entitled "Method and System for Down-converting Electromagnetic Signals," application Ser. No. 09/176,022, issued as U.S. Pat. No. 6,061,551 on May 9, 2000.

Alternatively, when the aliasing rate of the control signal **2006** is substantially equal to the frequency of the input signal **2004**, or substantially equal to a harmonic or sub-harmonic thereof, input signal **2004** is directly down-converted to a demodulated baseband signal. This is because, without modulation, the under-sampling pulses occur at the same point of subsequent cycles of the input signal **2004**. As a result, the under-samples form a constant output baseband signal. If the input signal **2004** includes lower frequency changes, such as amplitude, frequency, phase, etc., or any combination thereof, the charge stored during associated under-samples reflects the lower frequency changes, resulting in similar changes on the demodulated baseband signal. For example, to directly down-convert a 900 MHz input signal to a demodulated baseband signal (i.e., zero IF), the frequency of the control signal **2006** would be calculated as follows:

$$(\text{Freq}_{\text{input}} - \text{Freq}_{\text{IF}}) / n = \text{Freq}_{\text{control}}$$

$$(900 \text{ MHz} - 0 \text{ MHz}) / n = 900 \text{ MHz} / n$$

For  $n=0.5, 1, 2, 3, 4$ , etc., the frequency of the control signal **2006** should be substantially equal to 1.8 GHz, 900 MHz, 450 MHz, 300 MHz, 225 MHz, etc.

Exemplary time domain and frequency domain drawings, illustrating direct down-conversion of analog and digital AM

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and PM signals to demodulated baseband signals, and exemplary methods and systems thereof, are disclosed in the co-pending U.S. patent application entitled "Method and System for Down-converting Electromagnetic Signals," application Ser. No. 09/176,022, issued as U.S. Pat. No. 6,061,551 on May 9, 2000.

Alternatively, to down-convert an input FM signal to a non-FM signal, a frequency within the FM bandwidth must be down-converted to baseband (i.e., zero IF). As an example, to down-convert a frequency shift keying (FSK) signal (a sub-set of FM) to a phase shift keying (PSK) signal (a subset of PM), the mid-point between a lower frequency  $F_1$  and an upper frequency  $F_2$  (that is,  $[(F_1 + F_2)/2]$ ) of the FSK signal is down-converted to zero IF. For example, to down-convert an FSK signal having  $F_1$  equal to 899 MHz and  $F_2$  equal to 901 MHz, to a PSK signal, the aliasing rate of the control signal **2006** would be calculated as follows:

$$\text{Frequency of the input} = (F_1 + F_2) \div 2$$

$$= (899 \text{ MHz} + 901 \text{ MHz}) \div 2$$

$$= 900 \text{ MHz}$$

Frequency of the down-converted signal=0 (i.e., baseband)

$$(\text{Freq}_{\text{input}} - \text{Freq}_{\text{IF}})/n = \text{Freq}_{\text{control}}$$

$$(900 \text{ MHz} - 0 \text{ MHz})/n = 900 \text{ MHz}/n$$

For  $n=0.5, 1, 2, 3$ , etc., the frequency of the control signal **2006** should be substantially equal to 1.8 GHz, 900 MHz, 450 MHz, 300 MHz, 225 MHz, etc. The frequency of the down-converted PSK signal is substantially equal to one half the difference between the lower frequency  $F_1$  and the upper frequency  $F_2$ .

As another example, to down-convert a FSK signal to an amplitude shift keying (ASK) signal (a subset of AM), either the lower frequency  $F_1$  or the upper frequency  $F_2$  of the FSK signal is down-converted to zero IF. For example, to down-convert an FSK signal having  $F_1$  equal to 900 MHz and  $F_2$  equal to 901 MHz, to an ASK signal, the aliasing rate of the control signal **2006** should be substantially equal to:

$$(900 \text{ MHz} - 0 \text{ MHz})/n = 900 \text{ MHz}/n, \text{ or}$$

$$(901 \text{ MHz} - 0 \text{ MHz})/n = 901 \text{ MHz}/n.$$

For the former case of 900 MHz/ $n$ , and for  $n=0.5, 1, 2, 3, 4$ , etc., the frequency of the control signal **2006** should be substantially equal to 1.8 GHz, 900 MHz, 450 MHz, 300 MHz, 225 MHz, etc. For the latter case of 901 MHz/ $n$ , and for  $n=0.5, 1, 2, 3, 4$ , etc., the frequency of the control signal **2006** should be substantially equal to 1.802 GHz, 901 MHz, 450.5 MHz, 300.333 MHz, 225.25 MHz, etc. The frequency of the down-converted AM signal is substantially equal to the difference between the lower frequency  $F_1$  and the upper frequency  $F_2$  (i.e., 1 MHz).

Exemplary time domain and frequency domain drawings, illustrating down-conversion of FM signals to non-FM signals, and exemplary methods and systems thereof, are disclosed in the co-pending U.S. patent application entitled "Method and System for Down-converting Electromagnetic Signals," application Ser. No. 09/176,022, issued as U.S. Pat. No. 6,061,551 on May 9, 2000.

In an embodiment, the pulses of the control signal **2006** have negligible apertures that tend towards zero. This makes the UFT module **2002** a high input impedance device. This

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configuration is useful for situations where minimal disturbance of the input signal may be desired.

In another embodiment, the pulses of the control signal **2006** have non-negligible apertures that tend away from zero. This makes the UFT module **2002** a lower input impedance device. This allows the lower input impedance of the UFT module **2002** to be substantially matched with a source impedance of the input signal **2004**. This also improves the energy transfer from the input signal **2004** to the down-converted output signal **2012**, and hence the efficiency and signal to noise (s/n) ratio of UFT module **2002**.

Exemplary systems and methods for generating and optimizing the control signal **2006**, and for otherwise improving energy transfer and s/n ratio, are disclosed in the co-pending U.S. patent application entitled "Method and System for Down-converting Electromagnetic Signals," application Ser. No. 09/176,022, issued as U.S. Pat. No. 6,061,551 on May 9, 2000.

### 3. FREQUENCY UP-CONVERSION

The present invention is directed to systems and methods of frequency up-conversion, and applications of same.

An example frequency up-conversion system **300** is illustrated in FIG. 3. The frequency up-conversion system **300** is now described.

An input signal **302** (designated as "Control Signal" in FIG. 3) is accepted by a switch module **304**. For purposes of example only, assume that the input signal **302** is a FM input signal **606**, an example of which is shown in FIG. 6C. FM input signal **606** may have been generated by modulating information signal **602** onto oscillating signal **604** (FIGS. 6A and 6B). It should be understood that the invention is not limited to this embodiment. The information signal **602** can be analog, digital, or any combination thereof, and any modulation scheme can be used.

The output of switch module **304** is a harmonically rich signal **306**, shown for example in FIG. 6D as a harmonically rich signal **608**. The harmonically rich signal **608** has a continuous and periodic waveform.

FIG. 6E is an expanded view of two sections of harmonically rich signal **608**, section **610** and section **612**. The harmonically rich signal **608** may be a rectangular wave, such as a square wave or a pulse (although, the invention is not limited to this embodiment). For ease of discussion, the term "rectangular waveform" is used to refer to waveforms that are substantially rectangular. In a similar manner, the term "square wave" refers to those waveforms that are substantially square and it is not the intent of the present invention that a perfect square wave be generated or needed.

Harmonically rich signal **608** is comprised of a plurality of sinusoidal waves whose frequencies are integer multiples of the fundamental frequency of the waveform of the harmonically rich signal **608**. These sinusoidal waves are referred to as the harmonics of the underlying waveform, and the fundamental frequency is referred to as the first harmonic. FIG. 6F and FIG. 6G show separately the sinusoidal components making up the first, third, and fifth harmonics of section **610** and section **612**. (Note that in theory there may be an infinite number of harmonics; in this example, because harmonically rich signal **608** is shown as a square wave, there are only odd harmonics). Three harmonics are shown simultaneously (but not summed) in FIG. 6H.

The relative amplitudes of the harmonics are generally a function of the relative widths of the pulses of harmonically rich signal **306** and the period of the fundamental frequency, and can be determined by doing a Fourier analysis of har-

monically rich signal **306**. According to an embodiment of the invention, the input signal **606** may be shaped to ensure that the amplitude of the desired harmonic is sufficient for its intended use (e.g., transmission).

A filter **308** filters out any undesired frequencies (harmonics), and outputs an electromagnetic (EM) signal at the desired harmonic frequency or frequencies as an output signal **310**, shown for example as a filtered output signal **614** in FIG. 6I.

FIG. 4 illustrates an example universal frequency up-conversion (UFU) module **401**. The UFU module **401** includes an example switch module **304**, which comprises a bias signal **402**, a resistor or impedance **404**, a universal frequency translator (UFT) **450**, and a ground **408**. The UFT **450** includes a switch **406**. The input signal **302** (designated as "Control Signal" in FIG. 4) controls the switch **406** in the UFT **450**, and causes it to close and open. Harmonically rich signal **306** is generated at a node **405** located between the resistor or impedance **404** and the switch **406**.

Also in FIG. 4, it can be seen that an example filter **308** is comprised of a capacitor **410** and an inductor **412** shunted to a ground **414**. The filter is designed to filter out the undesired harmonics of harmonically rich signal **306**.

The invention is not limited to the UFU embodiment shown in FIG. 4.

For example, in an alternate embodiment shown in FIG. 5, an unshaped input signal **501** is routed to a pulse shaping module **502**. The pulse shaping module **502** modifies the unshaped input signal **501** to generate a (modified) input signal **302** (designated as the "Control Signal" in FIG. 5). The input signal **302** is routed to the switch module **304**, which operates in the manner described above. Also, the filter **308** of FIG. 5 operates in the manner described above.

The purpose of the pulse shaping module **502** is to define the pulse width of the input signal **302**. Recall that the input signal **302** controls the opening and closing of the switch **406** in switch module **304**. During such operation, the pulse width of the input signal **302** establishes the pulse width of the harmonically rich signal **306**. As stated above, the relative amplitudes of the harmonics of the harmonically rich signal **306** are a function of at least the pulse width of the harmonically rich signal **306**. As such, the pulse width of the input signal **302** contributes to setting the relative amplitudes of the harmonics of harmonically rich signal **306**.

Further details of up-conversion as described in this section are presented in pending U.S. application "Method and System for Frequency Up-Conversion," Ser. No. 09/176,154, filed Oct. 21, 1998, incorporated herein by reference in its entirety.

#### 4. ENHANCED SIGNAL RECEPTION

The present invention is directed to systems and methods of enhanced signal reception (ESR), and applications of same.

Referring to FIG. 21, transmitter **2104** accepts a modulating baseband signal **2102** and generates (transmitted) redundant spectrums **2106a-n**, which are sent over communications medium **2108**. Receiver **2112** recovers a demodulated baseband signal **2114** from (received) redundant spectrums **2110a-n**. Demodulated baseband signal **2114** is representative of the modulating baseband signal **2102**, where the level of similarity between the modulating baseband signal **2114** and the modulating baseband signal **2102** is application dependent.

Modulating baseband signal **2102** is preferably any information signal desired for transmission and/or reception. An

example modulating baseband signal **2202** is illustrated in FIG. 22A, and has an associated modulating baseband spectrum **2204** and image spectrum **2203** that are illustrated in FIG. 22B. Modulating baseband signal **2202** is illustrated as an analog signal in FIG. 22a, but could also be a digital signal, or combination thereof. Modulating baseband signal **2202** could be a voltage (or current) characterization of any number of real world occurrences, including for example and without limitation, the voltage (or current) representation for a voice signal.

Each transmitted redundant spectrum **2106a-n** contains the necessary information to substantially reconstruct the modulating baseband signal **2102**. In other words, each redundant spectrum **2106a-n** contains the necessary amplitude, phase, and frequency information to reconstruct the modulating baseband signal **2102**.

FIG. 22C illustrates example transmitted redundant spectrums **2206b-d**. Transmitted redundant spectrums **2206b-d** are illustrated to contain three redundant spectrums for illustration purposes only. Any number of redundant spectrums could be generated and transmitted as will be explained in following discussions.

Transmitted redundant spectrums **2206b-d** are centered at  $f_1$ , with a frequency spacing  $f_2$  between adjacent spectrums. Frequencies  $f_1$  and  $f_2$  are dynamically adjustable in real-time as will be shown below. FIG. 22D illustrates an alternate embodiment, where redundant spectrums **2208c,d** are centered on unmodulated oscillating signal **2209** at  $f_1$  (Hz). Oscillating signal **2209** may be suppressed if desired using, for example, phasing techniques or filtering techniques. Transmitted redundant spectrums are preferably above baseband frequencies as is represented by break **2205** in the frequency axis of FIGS. 22C and 22D.

Received redundant spectrums **2110a-n** are substantially similar to transmitted redundant spectrums **2106a-n**, except for the changes introduced by the communications medium **2108**. Such changes can include but are not limited to signal attenuation, and signal interference. FIG. 22E illustrates example received redundant spectrums **2210b-d**. Received redundant spectrums **2210b-d** are substantially similar to transmitted redundant spectrums **2206b-d**, except that redundant spectrum **2210c** includes an undesired jamming signal spectrum **2211** in order to illustrate some advantages of the present invention. Jamming signal spectrum **2211** is a frequency spectrum associated with a jamming signal. For purposes of this invention, a "jamming signal" refers to any unwanted signal, regardless of origin, that may interfere with the proper reception and reconstruction of an intended signal. Furthermore, the jamming signal is not limited to tones as depicted by spectrum **2211**, and can have any spectral shape, as will be understood by those skilled in the art(s).

As stated above, demodulated baseband signal **2114** is extracted from one or more of received redundant spectrums **2210b-d**. FIG. 22F illustrates example demodulated baseband signal **2212** that is, in this example, substantially similar to modulating baseband signal **2202** (FIG. 22A); where in practice, the degree of similarity is application dependent.

An advantage of the present invention should now be apparent. The recovery of modulating baseband signal **2202** can be accomplished by receiver **2112** in spite of the fact that high strength jamming signal(s) (e.g. jamming signal spectrum **2211**) exist on the communications medium. The intended baseband signal can be recovered because multiple redundant spectrums are transmitted, where each redundant spectrum carries the necessary information to reconstruct the baseband signal. At the destination, the redundant spectrums are isolated from each other so that the baseband signal can be

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recovered even if one or more of the redundant spectrums are corrupted by a jamming signal.

Transmitter **2104** will now be explored in greater detail. FIG. **23A** illustrates transmitter **2301**, which is one embodiment of transmitter **2104** that generates redundant spectrums configured similar to redundant spectrums **2206b-d**. Transmitter **2301** includes generator **2303**, optional spectrum processing module **2304**, and optional medium interface module **2320**. Generator **2303** includes: first oscillator **2302**, second oscillator **2309**, first stage modulator **2306**, and second stage modulator **2310**.

Transmitter **2301** operates as follows. First oscillator **2302** and second oscillator **2309** generate a first oscillating signal **2305** and second oscillating signal **2312**, respectively. First stage modulator **2306** modulates first oscillating signal **2305** with modulating baseband signal **2202**, resulting in modulated signal **2308**. First stage modulator **2306** may implement any type of modulation including but not limited to: amplitude modulation, frequency modulation, phase modulation, combinations thereof, or any other type of modulation. Second stage modulator **2310** modulates modulated signal **2308** with second oscillating signal **2312**, resulting in multiple redundant spectrums **2206a-n** shown in FIG. **23B**. Second stage modulator **2310** is preferably a phase modulator, or a frequency modulator, although other types of modulation may be implemented including but not limited to amplitude modulation. Each redundant spectrum **2206a-n** contains the necessary amplitude, phase, and frequency information to substantially reconstruct the modulating baseband signal **2202**.

Redundant spectrums **2206a-n** are substantially centered around  $f_1$ , which is the characteristic frequency of first oscillating signal **2305**. Also, each redundant spectrum **2206a-n** (except for **2206c**) is offset from  $f_1$  by approximately a multiple of  $f_2$  (Hz), where  $f_2$  is the frequency of the second oscillating signal **2312**. Thus, each redundant spectrum **2206a-n** is offset from an adjacent redundant spectrum by  $f_2$  (Hz). This allows the spacing between adjacent redundant spectrums to be adjusted (or tuned) by changing  $f_2$  that is associated with second oscillator **2309**. Adjusting the spacing between adjacent redundant spectrums allows for dynamic real-time tuning of the bandwidth occupied by redundant spectrums **2206a-n**.

In one embodiment, the number of redundant spectrums **2206a-n** generated by transmitter **2301** is arbitrary and may be unlimited as indicated by the "a-n" designation for redundant spectrums **2206a-n**. However, a typical communications medium will have a physical and/or administrative limitations (i.e. FCC regulations) that restrict the number of redundant spectrums that can be practically transmitted over the communications medium. Also, there may be other reasons to limit the number of redundant spectrums transmitted. Therefore, preferably, the transmitter **2301** will include an optional spectrum processing module **2304** to process the redundant spectrums **2206a-n** prior to transmission over communications medium **2108**.

In one embodiment, spectrum processing module **2304** includes a filter with a passband **2207** (FIG. **23C**) to select redundant spectrums **2206b-d** for transmission. This will substantially limit the frequency bandwidth occupied by the redundant spectrums to the passband **2207**. In one embodiment, spectrum processing module **2304** also up converts redundant spectrums and/or amplifies redundant spectrums prior to transmission over the communications medium **2108**. Finally, medium interface module **2320** transmits redundant spectrums over the communications medium **2108**. In one embodiment, communications medium **2108** is an over-the-

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air link and medium interface module **2320** is an antenna. Other embodiments for communications medium **2108** and medium interface module **2320** will be understood based on the teachings contained herein.

FIG. **23D** illustrates transmitter **2321**, which is one embodiment of transmitter **2104** that generates redundant spectrums configured similar to redundant spectrums **2208c-d** and unmodulated spectrum **2209**. Transmitter **2321** includes generator **2311**, spectrum processing module **2304**, and (optional) medium interface module **2320**. Generator **2311** includes: first oscillator **2302**, second oscillator **2309**, first stage modulator **2306**, and second stage modulator **2310**.

As shown in FIG. **23D**, many of the components in transmitter **2321** are similar to those in transmitter **2301**. However, in this embodiment, modulating baseband signal **2202** modulates second oscillating signal **2312**. Transmitter **2321** operates as follows. First stage modulator **2306** modulates second oscillating signal **2312** with modulating baseband signal **2202**, resulting in modulated signal **2322**. As described earlier, first stage modulator **2306** can effect any type of modulation including but not limited to: amplitude modulation frequency modulation, combinations thereof, or any other type of modulation. Second stage modulator **2310** modulates first oscillating signal **2304** with modulated signal **2322**, resulting in redundant spectrums **2208a-n**, as shown in FIG. **23E**. Second stage modulator **2310** is preferably a phase or frequency modulator, although other modulators could be used including but not limited to an amplitude modulator.

Redundant spectrums **2208a-n** are centered on unmodulated spectrum **2209** (at  $f_1$  Hz), and adjacent spectrums are separated by  $f_2$  Hz. The number of redundant spectrums **2208a-n** generated by generator **2311** is arbitrary and unlimited, similar to spectrums **2206a-n** discussed above. Therefore, optional spectrum processing module **2304** may also include a filter with passband **2325** to select, for example, spectrums **2208c,d** for transmission over communications medium **2108**. In addition, optional spectrum processing module **2304** may also include a filter (such as a bandstop filter) to attenuate unmodulated spectrum **2209**. Alternatively, unmodulated spectrum **2209** may be attenuated by using phasing techniques during redundant spectrum generation. Finally, (optional) medium interface module **2320** transmits redundant spectrums **2208c,d** over communications medium **2108**.

Receiver **2112** will now be explored in greater detail to illustrate recovery of a demodulated baseband signal from received redundant spectrums. FIG. **24A** illustrates receiver **2430**, which is one embodiment of receiver **2112**. Receiver **2430** includes optional medium interface module **2402**, down-converter **2404**, spectrum isolation module **2408**, and data extraction module **2414**. Spectrum isolation module **2408** includes filters **2410a-c**. Data extraction module **2414** includes demodulators **2416a-c**, error check modules **2420a-c**, and arbitration module **2424**. Receiver **2430** will be discussed in relation to the signal diagrams in FIGS. **24B-24I**.

In one embodiment, optional medium interface module **2402** receives redundant spectrums **2210b-d** (FIG. **22E**, and FIG. **24B**). Each redundant spectrum **2210b-d** includes the necessary amplitude, phase, and frequency information to substantially reconstruct the modulating baseband signal used to generate the redundant spectrums. However, in the present example, spectrum **2210c** also contains jamming signal **2211**, which may interfere with the recovery of a baseband signal from spectrum **2210c**. Down-converter **2404** down-converts received redundant spectrums **2210b-d** to lower intermediate frequencies, resulting in redundant spectrums **2406a-c** (FIG. **24C**). Jamming signal **2211** is also down-



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converted to jamming signal **2407**, as it is contained within redundant spectrum **2406b**. Spectrum isolation module **2408** includes filters **2410a-c** that isolate redundant spectrums **2406a-c** from each other (FIGS. **24D-24F**, respectively). Demodulators **2416a-c** independently demodulate spectrums **2406a-c**, resulting in demodulated baseband signals **2418a-c**, respectively (FIGS. **24G-24I**). Error check modules **2420a-c** analyze demodulated baseband signal **2418a-c** to detect any errors. In one embodiment, each error check module **2420a-c** sets an error flag **2422a-c** whenever an error is detected in a demodulated baseband signal. Arbitration module **2424** accepts the demodulated baseband signals and associated error flags, and selects a substantially error-free demodulated baseband signal (FIG. **24J**). In one embodiment, the substantially error-free demodulated baseband signal will be substantially similar to the modulating baseband signal used to generate the received redundant spectrums, where the degree of similarity is application dependent.

Referring to FIGS. **24G-I**, arbitration module **2424** will select either demodulated baseband signal **2418a** or **2418c**, because error check module **2420b** will set the error flag **2422b** that is associated with demodulated baseband signal **2418b**.

The error detection schemes implemented by the error detection modules include but are not limited to: cyclic redundancy check (CRC) and parity check for digital signals, and various error detections schemes for analog signal.

Further details of enhanced signal reception as described in this section are presented in pending U.S. application "Method and System for Ensuring Reception of a Communications Signal," Ser. No. 09/176,415, filed Oct. 21, 1998, issued as U.S. Pat. No. 6,061,555 on May 9, 2000.

## 5. UNIFIED DOWN-CONVERSION AND FILTERING

The present invention is directed to systems and methods of unified down-conversion and filtering (UDF), and applications of same.

In particular, the present invention includes a unified down-converting and filtering (UDF) module that performs frequency selectivity and frequency translation in a unified (i.e., integrated) manner. By operating in this manner, the invention achieves high frequency selectivity prior to frequency translation (the invention is not limited to this embodiment). The invention achieves high frequency selectivity at substantially any frequency, including but not limited to RF (radio frequency) and greater frequencies. It should be understood that the invention is not limited to this example of RF and greater frequencies. The invention is intended, adapted, and capable of working with lower than radio frequencies.

FIG. **17** is a conceptual block diagram of a UDF module **1702** according to an embodiment of the present invention. The UDF module **1702** performs at least frequency translation and frequency selectivity.

The effect achieved by the UDF module **1702** is to perform the frequency selectivity operation prior to the performance of the frequency translation operation. Thus, the UDF module **1702** effectively performs input filtering.

According to embodiments of the present invention, such input filtering involves a relatively narrow bandwidth. For example, such input filtering may represent channel select filtering, where the filter bandwidth may be, for example, 50 KHz to 150 KHz. It should be understood, however, that the invention is not limited to these frequencies. The invention is intended, adapted, and capable of achieving filter bandwidths of less than and greater than these values.

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In embodiments of the invention, input signals **1704** received by the UDF module **1702** are at radio frequencies. The UDF module **1702** effectively operates to input filter these RF input signals **1704**. Specifically, in these embodiments, the UDF module **1702** effectively performs input, channel select filtering of the RF input signal **1704**. Accordingly, the invention achieves high selectivity at high frequencies.

The UDF module **1702** effectively performs various types of filtering, including but not limited to bandpass filtering, low pass filtering, high pass filtering, notch filtering, all pass filtering, band stop filtering, etc., and combinations thereof.

Conceptually, the UDF module **1702** includes a frequency translator **1708**. The frequency translator **1708** conceptually represents that portion of the UDF module **1702** that performs frequency translation (down conversion).

The UDF module **1702** also conceptually includes an apparent input filter **1706** (also sometimes called an input filtering emulator). Conceptually, the apparent input filter **1706** represents that portion of the UDF module **1702** that performs input filtering.

In practice, the input filtering operation performed by the UDF module **1702** is integrated with the frequency translation operation. The input filtering operation can be viewed as being performed concurrently with the frequency translation operation. This is a reason why the input filter **1706** is herein referred to as an "apparent" input filter **1706**.

The UDF module **1702** of the present invention includes a number of advantages. For example, high selectivity at high frequencies is realizable using the UDF module **1702**. This feature of the invention is evident by the high Q factors that are attainable. For example, and without limitation, the UDF module **1702** can be designed with a filter center frequency  $k$  on the order of 900 MHz, and a filter bandwidth on the order of 50 KHz. This represents a Q of 18,000 (Q is equal to the center frequency divided by the bandwidth).

It should be understood that the invention is not limited to filters with high Q factors. The filters contemplated by the present invention may have lesser or greater Qs, depending on the application, design, and/or implementation. Also, the scope of the invention includes filters where Q factor as discussed herein is not applicable.

The invention exhibits additional advantages. For example, the filtering center frequency  $f_c$  of the UDF module **1702** can be electrically adjusted, either statically or dynamically.

Also, the UDF module **1702** can be designed to amplify input signals.

Further, the UDF module **1702** can be implemented without large resistors, capacitors, or inductors. Also, the UDF module **1702** does not require that tight tolerances be maintained on the values of its individual components, i.e., its resistors, capacitors, inductors, etc. As a result, the architecture of the UDF module **1702** is friendly to integrated circuit design techniques and processes.

The features and advantages exhibited by the UDF module **1702** are achieved at least in part by adopting a new technological paradigm with respect to frequency selectivity and translation. Specifically, according to the present invention, the UDF module **1702** performs the frequency selectivity operation and the frequency translation operation as a single, unified (integrated) operation. According to the invention, operations relating to frequency translation also contribute to the performance of frequency selectivity, and vice versa.

According to embodiments of the present invention, the UDF module generates an output signal from an input signal using samples/instances of the input signal and samples/instances of the output signal.

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More particularly, first, the input signal is under-sampled. This input sample includes information (such as amplitude, phase, etc.) representative of the input signal existing at the time the sample was taken.

As described further below, the effect of repetitively performing this step is to translate the frequency (that is, down-convert) of the input signal to a desired lower frequency, such as an intermediate frequency (IF) or baseband.

Next, the input sample is held (that is, delayed).

Then, one or more delayed input samples (some of which may have been scaled) are combined with one or more delayed instances of the output signal (some of which may have been scaled) to generate a current instance of the output signal.

Thus, according to a preferred embodiment of the invention, the output signal is generated from prior samples/instances of the input signal and/or the output signal. (It is noted that, in some embodiments of the invention, current samples/instances of the input signal and/or the output signal may be used to generate current instances of the output signal). By operating in this manner, the UDF module preferably performs input filtering and frequency down-conversion in a unified manner.

FIG. 19 illustrates an example implementation of the unified down-converting and filtering (UDF) module 1922. The UDF module 1922 performs the frequency translation operation and the frequency selectivity operation in an integrated, unified manner as described above, and as further described below.

In the example of FIG. 19, the frequency selectivity operation performed by the UDF module 1922 comprises a band-pass filtering operation according to EQ. 1, below, which is an example representation of a band-pass filtering transfer function.

$$VO = \alpha_1 z^{-1} VI - \beta_1 z^{-1} VO - \beta_0 z^{-2} VO \quad \text{EQ. 1}$$

It should be noted, however, that the invention is not limited to band-pass filtering. Instead, the invention effectively performs various types of filtering, including but not limited to bandpass filtering, low pass filtering, high pass filtering, notch filtering, all pass filtering, band stop filtering, etc., and combinations thereof. As will be appreciated, there are many representations of any given filter type. The invention is applicable to these filter representations. Thus, EQ. 1 is referred to herein for illustrative purposes only, and is not limiting.

The UDF module 1922 includes a down-convert and delay module 1924, first and second delay modules 1928 and 1930, first and second scaling modules 1932 and 1934, an output sample and hold module 1936, and an (optional) output smoothing module 1938. Other embodiments of the UDF module will have these components in different configurations, and/or a subset of these components, and/or additional components. For example, and without limitation, in the configuration shown in FIG. 19, the output smoothing module 1938 is optional.

As further described below, in the example of FIG. 19, the down-convert and delay module 1924 and the first and second delay modules 1928 and 1930 include switches that are controlled by a clock having two phases,  $\phi_1$  and  $\phi_2$ .  $\phi_1$  and  $\phi_2$  preferably have the same frequency, and are non-overlapping (alternatively, a plurality such as two clock signals having these characteristics could be used). As used herein, the term “non-overlapping” is defined as two or more signals where only one of the signals is active at any given time. In some embodiments, signals are “active” when they are high. In other embodiments, signals are active when they are low.

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Preferably, each of these switches closes on a rising edge of  $\phi_1$  or  $\phi_2$ , and opens on the next corresponding falling edge of  $\phi_1$  or  $\phi_2$ . However, the invention is not limited to this example. As will be apparent to persons skilled in the relevant art(s), other clock conventions can be used to control the switches.

In the example of FIG. 19, it is assumed that  $\alpha_1$  is equal to one. Thus, the output of the down-convert and delay module 1924 is not scaled. As evident from the embodiments described above, however, the invention is not limited to this example.

The example UDF module 1922 has a filter center frequency of 900.2 MHz and a filter bandwidth of 570 KHz. The pass band of the UDF module 1922 is on the order of 899.915 MHz to 900.485 MHz. The Q factor of the UDF module 1922 is approximately 1879 (i.e., 900.2 MHz divided by 570 KHz).

The operation of the UDF module 1922 shall now be described with reference to a Table 1802 (FIG. 18) that indicates example values at nodes in the UDF module 1922 at a number of consecutive time increments. It is assumed in Table 1802 that the UDF module 1922 begins operating at time  $t-1$ . As indicated below, the UDF module 1922 reaches steady state a few time units after operation begins. The number of time units necessary for a given UDF module to reach steady state depends on the configuration of the UDF module, and will be apparent to persons skilled in the relevant art(s) based on the teachings contained herein.

At the rising edge of  $\phi_1$  at time  $t-1$ , a switch 1950 in the down-convert and delay module 1924 closes. This allows a capacitor 1952 to charge to the current value of an input signal,  $VI_{t-1}$ , such that node 1902 is at  $VI_{t-1}$ . This is indicated by cell 1804 in FIG. 18. In effect, the combination of the switch 1950 and the capacitor 1952 in the down-convert and delay module 1924 operates to translate the frequency of the input signal  $VI$  to a desired lower frequency, such as IF or baseband. Thus, the value stored in the capacitor 1952 represents an instance of a down-converted image of the input signal  $VI$ .

The manner in which the down-convert and delay module 1924 performs frequency down-conversion is further described elsewhere in this application, and is additionally described in pending U.S. application “Method and System for Down-Converting Electromagnetic Signals,” Ser. No. 09/176,022, filed Oct. 21, 1998, issued as U.S. Pat. No. 6,061, 551 on May 9, 2000, which is herein incorporated by reference in its entirety.

Also at the rising edge of  $\phi_1$  at time  $t-1$ , a switch 1958 in the first delay module 1928 closes, allowing a capacitor 1960 to charge to  $VO_{t-1}$ , such that node 1906 is at  $VO_{t-1}$ . This is indicated by cell 1806 in Table 1802. (In practice,  $VO_{t-1}$  is undefined at this point. However, for ease of understanding,  $VO_{t-1}$  shall continue to be used for purposes of explanation.)

Also at the rising edge of  $\phi_1$  at time  $t-1$ , a switch 1966 in the second delay module 1930 closes, allowing a capacitor 1968 to charge to a value stored in a capacitor 1964. At this time, however, the value in capacitor 1964 is undefined, so the value in capacitor 1968 is undefined. This is indicated by cell 1807 in table 1802.

At the rising edge of  $\phi_2$  at time  $t-1$ , a switch 1954 in the down-convert and delay module 1924 closes, allowing a capacitor 1956 to charge to the level of the capacitor 1952. Accordingly, the capacitor 1956 charges to  $VI_{t-1}$ , such that node 1904 is at  $VI_{t-1}$ . This is indicated by cell 1810 in Table 1802.

The UDF module 1922 may optionally include a unity gain module 1990A between capacitors 1952 and 1956. The unity gain module 1990A operates as a current source to enable

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capacitor **1956** to charge without draining the charge from capacitor **1952**. For a similar reason, the UDF module **1922** may include other unity gain modules **1990B-1990G**. It should be understood that, for many embodiments and applications of the invention, these unity gain modules **1990A-1990G** are optional. The structure and operation of the unity gain modules **1990** will be apparent to persons skilled in the relevant art(s).

Also at the rising edge of  $\phi_2$  at time  $t-1$ , a switch **1962** in the first delay module **1928** closes, allowing a capacitor **1964** to charge to the level of the capacitor **1960**. Accordingly, the capacitor **1964** charges to  $VO_{t-1}$ , such that node **1908** is at  $VO_{t-1}$ . This is indicated by cell **1814** in Table **1802**.

Also at the rising edge of  $\phi_2$  at time  $t-1$ , a switch **1970** in the second delay module **1930** closes, allowing a capacitor **1972** to charge to a value stored in a capacitor **1968**. At this time, however, the value in capacitor **1968** is undefined, so the value in capacitor **1972** is undefined. This is indicated by cell **1815** in table **1802**.

At time  $t$ , at the rising edge of  $\phi_1$ , the switch **1950** in the down-convert and delay module **1924** closes. This allows the capacitor **1952** to charge to  $VI_t$ , such that node **1902** is at  $VI_t$ . This is indicated in cell **1816** of Table **1802**.

Also at the rising edge of  $\phi_1$  at time  $t$ , the switch **1958** in the first delay module **1928** closes, thereby allowing the capacitor **1960** to charge to  $VO_t$ . Accordingly, node **1906** is at  $VO_t$ . This is indicated in cell **1820** in Table **1802**.

Further at the rising edge of  $\phi_1$  at time  $t$ , the switch **1966** in the second delay module **1930** closes, allowing a capacitor **1968** to charge to the level of the capacitor **1964**. Therefore, the capacitor **1968** charges to  $VO_{t-1}$ , such that node **1910** is at  $VO_{t-1}$ . This is indicated by cell **1824** in Table **1802**.

At the rising edge of  $\phi_2$  at time  $t$ , the switch **1954** in the down-convert and delay module **1924** closes, allowing the capacitor **1956** to charge to the level of the capacitor **1952**. Accordingly, the capacitor **1956** charges to  $VI_t$ , such that node **1904** is at  $VI_t$ . This is indicated by cell **1828** in Table **1802**.

Also at the rising edge of  $\phi_2$  at time  $t$ , the switch **1962** in the first delay module **1928** closes, allowing the capacitor **1964** to charge to the level in the capacitor **1960**. Therefore, the capacitor **1964** charges to  $VO_t$ , such that node **1908** is at  $VO_t$ . This is indicated by cell **1832** in Table **1802**.

Further at the rising edge of  $\phi_2$  at time  $t$ , the switch **1970** in the second delay module **1930** closes, allowing the capacitor **1972** in the second delay module **1930** to charge to the level of the capacitor **1968** in the second delay module **1930**. Therefore, the capacitor **1972** charges to  $VO_{t-1}$ , such that node **1912** is at  $VO_{t-1}$ . This is indicated in cell **1836** of FIG. **18**.

At time  $t+1$ , at the rising edge of  $\phi_1$ , the switch **1950** in the down-convert and delay module **1924** closes, allowing the capacitor **1952** to charge to  $VI_{t+1}$ . Therefore, node **1902** is at  $VI_{t+1}$ , as indicated by cell **1838** of Table **1802**.

Also at the rising edge of  $\phi_1$  at time  $t+1$ , the switch **1958** in the first delay module **1928** closes, allowing the capacitor **1960** to charge to  $VO_{t+1}$ . Accordingly, node **1906** is at  $VO_{t+1}$ , as indicated by cell **1842** in Table **1802**.

Further at the rising edge of  $\phi_1$  at time  $t+1$ , the switch **1966** in the second delay module **1930** closes, allowing the capacitor **1968** to charge to the level of the capacitor **1964**. Accordingly, the capacitor **1968** charges to  $VO_t$ , as indicated by cell **1846** of Table **1802**.

In the example of FIG. **19**, the first scaling module **1932** scales the value at node **1908** (i.e., the output of the first delay module **1928**) by a scaling factor of  $-0.1$ . Accordingly, the value present at node **1914** at time  $t+1$  is  $-0.1*VO_t$ . Similarly, the second scaling module **1934** scales the value present at

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node **1912** (i.e., the output of the second scaling module **1930**) by a scaling factor of  $-0.8$ . Accordingly, the value present at node **1916** is  $-0.8*VO_{t-1}$  at time  $t+1$ .

At time  $t+1$ , the values at the inputs of the summer **1926** are:  $VI_t$  at node **1904**,  $-0.1*VO_t$  at node **1914**, and  $-0.8*VO_{t-1}$  at node **1916** (in the example of FIG. **19**, the values at nodes **1914** and **1916** are summed by a second summer **1925**, and this sum is presented to the summer **1926**). Accordingly, at time  $t+1$ , the summer generates a signal equal to  $VI_t - 0.1*VO_t - 0.8*VO_{t-1}$ .

At the rising edge of  $\phi_1$  at time  $t+1$ , a switch **1991** in the output sample and hold module **1936** closes, thereby allowing a capacitor **1992** to charge to  $VO_{t+1}$ . Accordingly, the capacitor **1992** charges to  $VO_{t+1}$ , which is equal to the sum generated by the adder **1926**. As just noted, this value is equal to:  $VI_t - 0.1*VO_t - 0.8*VO_{t-1}$ . This is indicated in cell **1850** of Table **1802**. This value is presented to the optional output smoothing module **1938**, which smooths the signal to thereby generate the instance of the output signal  $VO_{t+1}$ . It is apparent from inspection that this value of  $VO_{t+1}$  is consistent with the band pass filter transfer function of EQ. 1.

Further details of unified down-conversion and filtering as described in this section are presented in pending U.S. application "Integrated Frequency Translation And Selectivity," Ser. No. 09/175,966, filed Oct. 21, 1998, issued as U.S. Pat. No. 6,049,706 on Apr. 11, 2000, incorporated herein by reference in its entirety.

## 6. EXAMPLE APPLICATION EMBODIMENTS OF THE INVENTION

As noted above, the UFT module of the present invention is a very powerful and flexible device. Its flexibility is illustrated, in part, by the wide range of applications in which it can be used. Its power is illustrated, in part, by the usefulness and performance of such applications.

Example applications of the UFT module were described above. In particular, frequency down-conversion, frequency up-conversion, enhanced signal reception, and unified down-conversion and filtering applications of the UFT module were summarized above, and are further described below. These applications of the UFT module are discussed herein for illustrative purposes. The invention is not limited to these example applications. Additional applications of the UFT module will be apparent to persons skilled in the relevant art(s), based on the teachings contained herein.

For example, the present invention can be used in applications that involve frequency down-conversion. This is shown in FIG. **1C**, for example, where an example UFT module **115** is used in a down-conversion module **114**. In this capacity, the UFT module **115** frequency down-converts an input signal to an output signal. This is also shown in FIG. **7**, for example, where an example UFT module **706** is part of a down-conversion module **704**, which is part of a receiver **702**.

The present invention can be used in applications that involve frequency up-conversion. This is shown in FIG. **1D**, for example, where an example UFT module **117** is used in a frequency up-conversion module **116**. In this capacity, the UFT module **117** frequency up-converts an input signal to an output signal. This is also shown in FIG. **8**, for example, where an example UFT module **806** is part of up-conversion module **804**, which is part of a transmitter **802**.

The present invention can be used in environments having one or more transmitters **902** and one or more receivers **906**, as illustrated in FIG. **9**. In such environments, one or more of the transmitters **902** may be implemented using a UFT mod-

ule, as shown for example in FIG. 8. Also, one or more of the receivers 906 may be implemented using a UFT module, as shown for example in FIG. 7.

The invention can be used to implement a transceiver. An example transceiver 1002 is illustrated in FIG. 10. The transceiver 1002 includes a transmitter 1004 and a receiver 1008. Either the transmitter 1004 or the receiver 1008 can be implemented using a UFT module. Alternatively, the transmitter 1004 can be implemented using a UFT module 1006, and the receiver 1008 can be implemented using a UFT module 1010. This embodiment is shown in FIG. 10.

Another transceiver embodiment according to the invention is shown in FIG. 11. In this transceiver 1102, the transmitter 1104 and the receiver 1108 are implemented using a single UFT module 1106. In other words, the transmitter 1104 and the receiver 1108 share a UFT module 1106.

As described elsewhere in this application, the invention is directed to methods and systems for enhanced signal reception (ESR). Various ESR embodiments include an ESR module (transmit) in a transmitter 1202, and an ESR module (receive) in a receiver 1210. An example ESR embodiment configured in this manner is illustrated in FIG. 12.

The ESR module (transmit) 1204 includes a frequency up-conversion module 1206. Some embodiments of this frequency up-conversion module 1206 may be implemented using a UFT module, such as that shown in FIG. 1D.

The ESR module (receive) 1212 includes a frequency down-conversion module 1214. Some embodiments of this frequency down-conversion module 1214 may be implemented using a UFT module, such as that shown in FIG. 1C.

As described elsewhere in this application, the invention is directed to methods and systems for unified down-conversion and filtering (UDF). An example unified down-conversion and filtering module 1302 is illustrated in FIG. 13. The unified down-conversion and filtering module 1302 includes a frequency down-conversion module 1304 and a filtering module 1306. According to the invention, the frequency down-conversion module 1304 and the filtering module 1306 are implemented using a UFT module 1308, as indicated in FIG. 13.

Unified down-conversion and filtering according to the invention is useful in applications involving filtering and/or frequency down-conversion. This is depicted, for example, in FIGS. 15A-15F. FIGS. 15A-15C indicate that unified down-conversion and filtering according to the invention is useful in applications where filtering precedes, follows, or both precedes and follows frequency down-conversion. FIG. 15D indicates that a unified down-conversion and filtering module 1524 according to the invention can be utilized as a filter 1522 (i.e., where the extent of frequency down-conversion by the down-converter in the unified down-conversion and filtering module 1524 is minimized). FIG. 15E indicates that a unified down-conversion and filtering module 1528 according to the invention can be utilized as a down-converter 1526 (i.e., where the filter in the unified down-conversion and filtering module 1528 passes substantially all frequencies). FIG. 15F illustrates that the unified down-conversion and filtering module 1532 can be used as an amplifier. It is noted that one or more UDF modules can be used in applications that involve at least one or more of filtering, frequency translation, and amplification.

For example, receivers, which typically perform filtering, down-conversion, and filtering operations, can be implemented using one or more unified down-conversion and filtering modules. This is illustrated, for example, in FIG. 14.

The methods and systems of unified down-conversion and filtering of the invention have many other applications. For example, as discussed herein, the enhanced signal reception

(ESR) module (receive) operates to down-convert a signal containing a plurality of spectrums. The ESR module (receive) also operates to isolate the spectrums in the down-converted signal, where such isolation is implemented via filtering in some embodiments. According to embodiments of the invention, the ESR module (receive) is implemented using one or more unified down-conversion and filtering (UDF) modules. This is illustrated, for example, in FIG. 16. In the example of FIG. 16, one or more of the UDF modules 1610, 1612, 1614 operates to down-convert a received signal. The UDF modules 1610, 1612, 1614 also operate to filter the down-converted signal so as to isolate the spectrum(s) contained therein. As noted above, the UDF modules 1610, 1612, 1614 are implemented using the universal frequency translation (UFT) modules of the invention.

The invention is not limited to the applications of the UFT module described above. For example, and without limitation, subsets of the applications (methods and/or structures) described herein (and others that would be apparent to persons skilled in the relevant art(s) based on the herein teachings) can be associated to form useful combinations.

For example, transmitters and receivers are two applications of the UFT module. FIG. 10 illustrates a transceiver 1002 that is formed by combining these two applications of the UFT module, i.e., by combining a transmitter 1004 with a receiver 1008.

Also, ESR (enhanced signal reception) and unified down-conversion and filtering are two other applications of the UFT module. FIG. 16 illustrates an example where ESR and unified down-conversion and filtering are combined to form a modified enhanced signal reception system.

The invention is not limited to the example applications of the UFT module discussed herein. Also, the invention is not limited to the example combinations of applications of the UFT module discussed herein. These examples were provided for illustrative purposes only, and are not limiting. Other applications and combinations of such applications will be apparent to persons skilled in the relevant art(s) based on the teachings contained herein. Such applications and combinations include, for example and without limitation, applications/combinations comprising and/or involving one or more of: (1) frequency translation; (2) frequency down-conversion; (3) frequency up-conversion; (4) receiving; (5) transmitting; (6) filtering; and/or (7) signal transmission and reception in environments containing potentially jamming signals.

Additional example applications are described below.

### 6.1 Data Communication

The invention is directed to data communication among data processing devices. For example, and without limitation, the invention is directed to computer networks such as, for example, local area networks (LANs), wide area networks (WANs), including wireless LANs (WLANs) and wireless WANs, modulator/demodulators (modems), including wireless modems, etc.

FIG. 25 illustrates an example environment 2502 wherein computers 2504, 2512, and 2526 communicate with one another via a computer network 2534. It is noted that the invention is not limited to computers, but encompasses any data processing and/or communications device or other device where communications with external devices is desired. Also, the invention includes but is not limited to WLAN client (also called mobile terminals, and/or stations) and infrastructure devices (also called access points). In the example of FIG. 25, computer 2504 is communicating with

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the network **2534** via a wired link, whereas computers **2512** and **2526** are communicating with the network **2534** via wireless links.

In the teachings contained herein, for illustrative purposes, a link may be designated as being a wired link or a wireless link. Such designations are for example purposes only, and are not limiting. A link designated as being wireless may alternatively be wired. Similarly, a link designated as being wired may alternatively be wireless. This is applicable throughout the entire application.

The computers **2504**, **2512** and **2526** each include an interface **2506**, **2514**, and **2528**, respectively, for communicating with the network **2534**. The interfaces **2506**, **2514**, and **2528** include transmitters **2508**, **2516**, and **2530** respectively. Also, the interfaces **2506**, **2514** and **2528** include receivers **2510**, **2518**, and **2532** respectively. In embodiments of the invention, the transmitters **2508**, **2516** and **2530** are implemented using UFT modules for performing frequency up-conversion operations (see, for example, FIG. **8**). In embodiments, the receivers **2510**, **2518** and **2532** are implemented using UFT modules for performing frequency down-conversion operations (see, for example, FIG. **7**).

As noted above, the computers **2512** and **2526** interact with the network **2534** via wireless links. In embodiments of the invention, the interfaces **2514**, **2528** in computers **2512**, **2526** represent modulator/demodulators (modems).

In embodiments, the network **2534** includes an interface or modem **2520** for communicating with the modems **2514**, **2528** in the computers **2512**, **2526**. In embodiments, the interface **2520** includes a transmitter **2522**, and a receiver **2524**. Either or both of the transmitter **2522**, and the receiver **2524** are implemented using UFT modules for performing frequency translation operations (see, for example, FIGS. **7** and **8**).

In alternative embodiments, one or more of the interfaces **2506**, **2514**, **2520**, and **2528** are implemented using transceivers that employ one or more UFT modules for performing frequency translation operations (see, for example, FIGS. **10** and **11**).

FIG. **26** illustrates another example data communication embodiment **2602**. Each of a plurality of computers **2604**, **2612**, **2614** and **2616** includes an interface, such as an interface **2606** shown in the computer **2604**. It should be understood that the other computers **2612**, **2614**, **2616** also include an interface such as an interface **2606**. The computers **2604**, **2612**, **2614** and **2616** communicate with each other via interfaces **2606** and wireless or wired links, thereby collectively representing a data communication network.

The interfaces **2606** may represent any computer interface or port, such as but not limited to a high speed internal interface, a wireless serial port, a wireless PS2 port, a wireless USB port, PCMCIA port, etc.

The interface **2606** includes a transmitter **2608** and a receiver **2610**. In embodiments of the invention, either or both of the transmitter **2608** and the receiver **2610** are implemented using UFT modules for frequency up-conversion and down-conversion (see, for example, FIGS. **7** and **8**). Alternatively, the interfaces **2806** can be implemented using a transceiver having one or more UFT modules for performing frequency translation operations (see, for example, FIGS. **10** and **11**).

FIGS. **33-38** illustrate other scenarios envisioned and encompassed by the invention. FIG. **33** illustrates a data processing environment **3302** wherein a wired network, such as an Ethernet network **3304**, is linked to another network, such as a WLAN **3306**, via a wireless link **3308**. The wireless link

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**3308** is established via interfaces **3310**, **3312** which are preferably implemented using universal frequency translation modules.

FIGS. **35-38** illustrate that the present invention supports WLANs that are located in one or more buildings or over any defined geographical area, as shown in FIGS. **35-38**.

The invention includes multiple networks linked together. The invention also envisions wireless networks conforming to any known or custom standard or specification. This is shown in FIG. **34**, for example, where any combination of WLANs conforming to any WLAN standard or configuration, such as IEEE 802.11 and Bluetooth (or other relatively short range communication specification or standard), any WAN cellular or telephone standard or specification, any type of radio links, any custom standard or specification, etc., or combination thereof, can be implemented using the universal frequency translation technology described herein. Also, any combination of these networks may be coupled together, as illustrated in FIG. **34**.

The invention supports WLANs that are located in one or multiple buildings, as shown in FIGS. **35** and **36**. The invention also supports WLANs that are located in an area including and external to one or more buildings, as shown in FIG. **37**. In fact, the invention is directed to networks that cover any defined geographical area, as shown in FIG. **38**. In the embodiments described above, wireless links are preferably established using WLAN interfaces as described herein.

More generally, the invention is directed to WLAN client devices and WLAN infrastructure devices. "WLAN Client Devices" refers to, for example, any data processing and/or communication devices in which wired or wireless communication functionality is desired, such as but not limited to computers, personal data assistants (PDAs), automatic identification data collection devices (such as bar code scanners/readers, electronic article surveillance readers, and radio frequency identification readers), telephones, network devices, etc., and combinations thereof. "WLAN Infrastructure Devices" refers to, for example, Access Points and other devices used to provide the ability for WLAN Client Devices (as well as potentially other devices) to connect to wired and/or wireless networks and/or to provide the network functionality of a WLAN. "WLAN" refers to, for example, a Wireless Local Area Network that is implemented according to and that operates within WLAN standards and/or specifications, such as but not limited to IEEE 802.11, IEEE 802.11a, IEEE 802.11b, HomeRF, Proxim Range LAN, Proxim Range LAN2, Symbol Spectrum 1, Symbol Spectrum 24 as it existed prior to adoption of IEEE 802.11, HiperLAN1, or HiperLAN2. WLAN client devices and/or WLAN infrastructure devices may operate in a multi-mode capacity. For example, a device may include WLAN and WAN functionality. Another device may include WLAN and short range communication (such as but not limited to Blue Tooth) functionality. Another device may include WLAN and WAN and short range communication functionality. It is noted that the above definitions and examples are provided for illustrative purposes, and are not limiting. Equivalents to that described above will be apparent to persons skilled in the relevant art(s) based on the teachings contained herein.

6.1.1. Example Implementations: Interfaces, Wireless Modems, Wireless LANs, etc.

The present invention is now described as implemented in an interface, such as a wireless modem or other device (such as client or infrastructure device), which can be utilized to implement or interact with a wireless local area network (WLAN) or wireless wide area network (WWAN), for example. In an embodiment, the present invention is imple-

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mented in a WLAN to support IEEE WLAN Standard 802.11, but this embodiment is mentioned for illustrative purposes only. The invention is not limited to this standard.

Conventional wireless modems are described in, for example, U.S. Pat. No. 5,764,693, titled, "Wireless Radio Modem with Minimal Inter-Device RF Interference," incorporated herein by reference in its entirety. The present invention replaces a substantial portion of conventional wireless modems with one or more universal frequency translators (UFTs). The resultant improved wireless modem consumes less power than conventional wireless modems and is easier and less expensive to design and build. A wireless modem in accordance with the present invention can be implemented in a PC-MCIA card or within a main housing of a computer, for example.

FIG. 27 illustrates an example block diagram of a computer system 2710, which can be wirelessly coupled to a LAN, as illustrated in FIGS. 25 and 26. The computer system 2710 includes an interface 2714 and an antenna 2712. The interface 2714 includes a transmitter module 2716 that receives information from a digital signal processor (DSP) 2720, and modulates and up-converts the information for transmission from the antenna 2712. The interface 2714 also includes a receiver module 2718 that receives modulated carrier signals via the antenna 2712. The receiver module 2718 down-converts and demodulates the modulated carrier signals to baseband information, and provides the baseband information to the DSP 2720. The DSP 2720 can include a central processing unit (CPU) and other components of the computer 2712. Conventionally, the interface 2714 is implemented with heterodyne components.

FIG. 28 illustrates an example interface 2810 implemented with heterodyne components. The interface 2810 includes a transmitter module 2812 and a receiver module 2824. The receiver module 2824 includes an RF section 2830, one or more IF sections 2828, a demodulator section 2826, an optional analog to digital (A/D) converter 2834, and a frequency generator/synthesizer 2832. The transmitter module 2812 includes an optional digital to analog (D/A) converter 2822, a modulator section 2818, one or more IF sections 2816, an RF section 2814, and a frequency generator/synthesizer 2820. Operation of the interface 2810 will be apparent to one skilled in the relevant art(s), based on the description herein.

FIG. 29 illustrates an example in-phase/quadrature-phase (I/Q) interface 2910 implemented with heterodyne components. I/Q implementations allow two channels of information to be communicated on a carrier signal and thus can be utilized to increase data transmission.

The interface 2910 includes a transmitter module 2912 and a receiver module 2934. The receiver module 2934 includes an RF section 2936, one or more IF sections 2938, an I/Q demodulator section 2940, an optional A/D converter 2944, and a frequency generator/synthesizer 2942. The I/Q demodulator section 2940 includes a signal splitter 2946, mixers 2948, and a phase shifter 2950. The signal splitter 2946 provides a received signal to the mixers 2948. The phase shifter 2950 operates the mixers 2948 ninety degrees out of phase with one another to generate I and Q information channels 2952 and 2954, respectively, which are provided to a DSP 2956 through the optional A/D converter 2944.

The transmitter module 2912 includes an optional D/A converter 2922, an I/Q modulator section 2918, one or more IF sections 2916, an RF section 2914, and a frequency generator/synthesizer 2920. The I/Q modulator section 2918 includes mixers 2924, a phase shifter 2926, and a signal combiner 2928. The phase shifter 2926 operates the mixers

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2924 ninety degrees out of phase with one another to generate I and Q modulated information signals 2930 and 2932, respectively, which are combined by the signal combiner 2928. The IF section(s) 2916 and RF section 2914 up-convert the combined I and Q modulated information signals 2930 and 2932 to RF for transmission by the antenna, in a manner well known in the relevant art(s).

Heterodyne implementations, such as those illustrated in FIGS. 28 and 29, are expensive and difficult to design, manufacture and tune. In accordance with the present invention, therefore, the interface 2714 (FIG. 27) is preferably implemented with one or more universal frequency translation (UFT) modules, such as the UFT module 102 (FIG. 1A). Thus previously described benefits of the present invention are obtained in wireless modems, WLANs, etc.

FIG. 30 illustrates an example block diagram embodiment of the interface 2714 that is associated with a computer or any other data processing and/or communications device. In FIG. 30, the receiver module 2718 includes a universal frequency down-converter (UFD) module 3014 and an optional analog to digital (A/D) converter 3016, which converts an analog output from the UFD 3014 to a digital format for the DSP 2720. The transmitter module 2716 includes an optional modulator 3012 and a universal frequency up-converter (UFU) module 3010. The optional modulator 3012 can be a variety of types of modulators, including conventional modulators. Alternatively, the UFU module 3010 includes modulator functionality. The example implementation of FIG. 30 operates substantially as described above and in co-pending U.S. patent applications titled, "Method and System for Down-Converting Electromagnetic Signals," Ser. No. 09/176,022, filed Oct. 21, 1998, issued as U.S. Pat. No. 6,061,551 on May 9, 2000, and "Method and System for Frequency Up-Conversion," Ser. No. 09/176,154, filed Oct. 21, 1998, issued as U.S. Pat. No. 6,091,940 on Jul. 18, 2000, as well as other cited documents.

FIG. 31 illustrates an example implementation of the interface 2714 illustrated in FIG. 30, wherein the receiver UFD 3014 includes a UFT module 3112, and the transmitter UFU 3010 includes a universal frequency translation (UFT) module 3110. This example implementation operates substantially as described above and in co-pending U.S. patent applications titled, "Method and System for Down-Converting Electromagnetic Signals," Ser. No. 09/176,022, filed Oct. 21, 1998, issued as U.S. Pat. No. 6,061,551 on May 9, 2000, and "Method and System for Frequency Up-Conversion," Ser. No. 09/176,154, filed Oct. 21, 1998, "Method and System for Frequency Up-Conversion," Ser. No. 09/176,154, filed Oct. 21, 1998, issued as U.S. Pat. No. 6,091,940 on Jul. 18, 2000, as well as other cited documents.

FIG. 32 illustrates an example I/Q implementation of the interface module 2710. Other I/Q implementations are also contemplated and are within the scope of the present invention.

In the example of FIG. 32, the receiver UFD module 3014 includes a signal divider 3228 that provides a received I/Q modulated carrier signal 3230 between a third UFT module 3224 and a fourth UFT module 3226. A phase shifter 3232, illustrated here as a 90 degree phase shifter, controls the third and fourth UFT modules 3224 and 3226 to operate 90 degrees out of phase with one another. As a result, the third and fourth UFT modules 3224 and 3226 down-convert and demodulate the received I/Q modulated carrier signal 3230, and output I and Q channels 3234 and 3236, respectively, which are provided to the DSP 2720 through the optional A/D converter 3016.

In the example of FIG. 32, the transmitter UFU module 3010 includes first and second UFT modules 3212 and 3214 and a phase shifter 3210, which is illustrated here as a 90 degree phase shifter. The phase shifter 3210 receives a lower frequency modulated carrier signal 3238 from the modulator 3012. The phase shifter 3210 controls the first and second UFT modules 3212 and 3214 to operate 90 degrees out of phase with one another. The first and second UFT modules 3212 and 3214 up-convert the lower frequency modulated carrier signal 3238, which are output as higher frequency modulated I and Q carrier channels 3218 and 3220, respectively. A signal combiner 3216 combines the higher frequency modulated I and Q carrier channels 3218 and 3220 into a single higher frequency modulated I/Q carrier signal 3222 for transmitting by the antenna 2712.

The example implementations of the interfaces described above, and variations thereof, can also be used to implement network interfaces, such as the network interface 2520 illustrated in FIG. 25.

#### 6.1.2. Example Modifications

The RF modem applications, WLAN applications, etc., described herein, can be modified by incorporating one or more of the enhanced signal reception (ESR) techniques described herein. Use of ESR embodiments with the network embodiments described herein will be apparent to persons skilled in the relevant art(s) based on the teachings contained herein.

The RF modem applications, WLAN applications, etc., described herein can be enhanced by incorporating one or more of the unified down-conversion and filtering (UDF) techniques described herein. Use of UDF embodiments with the network embodiments described herein will be apparent to persons skilled in the relevant art(s) based on the teachings contained herein.

#### 6.2. Other Example Applications

The application embodiments described above are provided for purposes of illustration. These applications and embodiments are not intended to limit the invention. Alternate and additional applications and embodiments, differing slightly or substantially from those described herein, will be apparent to persons skilled in the relevant art(s) based on the teachings contained herein. For example, such alternate and additional applications and embodiments include combinations of those described above. Such combinations will be apparent to persons skilled in the relevant art(s) based on the herein teachings.

### 7.0. EXAMPLE WLAN IMPLEMENTATION EMBODIMENTS

#### 7.1 Architecture

FIG. 39 is a block diagram of a WLAN interface 3902 (also referred to as a WLAN modem herein) according to an embodiment of the invention. The WLAN interface/modem 3902 includes an antenna 3904, a low noise amplifier or power amplifier (LNA/PA) 3904, a receiver 3906, a transmitter 3910, a control signal generator 3908, a demodulator/modulator facilitation module 3912, and a media access controller (MAC) interface 3914. Other embodiments may include different elements. The MAC interface 3914 couples the WLAN interface/modem 3902 to a computer 3916 or other data processing device. The computer 3916 preferably includes a MAC 3918.

The WLAN interface/modem 3902 represents a transmit and receive application that utilizes the universal frequency translation technology described herein. It also represents a zero IF (or direct-to-data) WLAN architecture.

The WLAN interface/modem 3902 also represents a vector modulator and a vector demodulator using the universal frequency translation (UFT) technology described herein. Use of the UFT technology enhances the flexibility of the WLAN application (i.e., makes it universal).

In the embodiment shown in FIG. 39, the WLAN interface/modem 3902 is compliant with WLAN standard IEEE 802.11. However, the invention is not limited to this standard. The invention is applicable to any communication standard or specification, as will be appreciated by persons skilled in the relevant art(s) based on the teachings contained herein. Any modifications to the invention to operate with other standards or specifications will be apparent to persons skilled in the relevant art(s) based on the teachings contained herein.

In the embodiment shown in FIG. 39, the WLAN interface/modem 3902 provides half duplex communication. However, the invention is not limited to this communication mode. The invention is applicable and directed to other communication modes, as will be appreciated by persons skilled in the relevant art(s) based on the teachings contained herein.

In the embodiment shown in FIG. 39, the modulation/demodulation performed by the WLAN interface/modem 3902 is preferably direct sequence spread spectrum QPSK (quadrature phase shift keying) with differential encoding. However, the invention is not limited to this modulation/demodulation mode. The invention is applicable and directed to other modulation and demodulation modes, such as but not limited to those described herein, as well as frequency hopping according to IEEE 802.11, OFDM (orthogonal frequency division multiplexing), as well as others. These modulation/demodulation modes will be appreciated by persons skilled in the relevant art(s) based on the teachings contained herein.

The operation of the WLAN interface/modem 3902 when receiving shall now be described.

Signals 3922 received by the antenna 3903 are amplified by the LNA/PA 3904. The amplified signals 3924 are down-converted and demodulated by the receiver 3906. The receiver 3906 outputs I signal 3926 and Q signal 3928.

FIG. 40 illustrates an example receiver 3906 according to an embodiment of the invention. It is noted that the receiver 3906 shown in FIG. 40 represents a vector modulator. The "receiving" function performed by the WLAN interface/modem 3902 can be considered to be all processing performed by the WLAN interface/modem 3902 from the LNA/PA 3904 to generation of baseband information.

Signal 3924 is split by a 90 degree splitter 4001 to produce an I signal 4006A and Q signal 4006B that are preferably 90 degrees apart in phase. I and Q signals 4006A, 4006B are down-converted by UFD (universal frequency down-conversion) modules 4002A, 4002B. The UFD modules 4002A, 4002B output down-converted I and Q signals 3926, 3928. The UFD modules 4002A, 4002B each includes at least one UFT (universal frequency translation) module 4004A. UFD and UFT modules are described above. An example implementation of the receiver 3906 (vector demodulator) is shown in FIG. 53. An example BOM list for the receiver 3906 of FIG. 53 is shown in FIG. 54.

The demodulator/modulator facilitation module 3912 receives the I and Q signals 3926, 3928. The demodulator/modulator facilitation module 3912 amplifies and filters the I and Q signals 3926, 3928. The demodulator/modulator facilitation module 3912 also performs automatic gain control



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(AGC) functions. The AGC function is coupled with the universal frequency translation technology described herein. The demodulator/modulator facilitation module 3912 outputs processed I and Q signals 3930, 3932.

The MAC interface 3914 receives the processed I and Q signals 3930, 3932. The MAC interface 3914 preferably includes a baseband processor. The MAC interface 3914 preferably performs functions such as combining the I and Q signals 3930, 3932, and arranging the data according to the protocol/file format being used. Other functions performed by the MAC interface 3914 and the baseband processor contained therein will be apparent to persons skilled in the relevant art(s) based on the teachings contained herein. The MAC interface 3914 outputs the baseband information signal, which is received and processed by the computer 3916 in an implementation and application specific manner.

In the example embodiment of FIG. 39, the demodulation function is distributed among the receiver 3906, the demodulator/modulator facilitation module 3912, and a baseband processor contained in the MAC interface 3914. The functions collectively performed by these components include, but are not limited to, despreading the information, differentially decoding the information, tracking the carrier phase, descrambling, recreating the data clock, and combining the I and Q signals. The invention is not limited to this arrangement. These demodulation-type functions can be centralized in a single component, or distributed in other ways.

The operation of the WLAN interface/modem 3902 when transmitting shall now be described.

A baseband information signal 3936 is received by the MAC interface 3914 from the computer 3916. The MAC interface 3914 preferably performs functions such as splitting the baseband information signal to form I and Q signals 3930, 3932, and arranging the data according to the protocol/file format being used. Other functions performed by the MAC interface 3914 and the baseband processor contained therein will be apparent to persons skilled in the relevant art(s) based on the teachings contained herein.

The demodulator/modulator facilitation module 3912 filters and amplifies the I and Q signals 3930, 3932. The demodulator/modulator facilitation module 3912 outputs processed I and Q signals 3942, 3944. Preferably, at least some filtering and/or amplifying components in the demodulator/modulator facilitation module 3912 are used for both the transmit and receive paths.

The transmitter 3910 up-converts the processed I and Q signals 3942, 3944, and combines the up-converted I and Q signals. This up-converted/combined signal is amplified by the LNA/PA 3904, and then transmitted via the antenna 3904.

FIG. 41 illustrates an example transmitter 3910 according to an embodiment of the invention. The device in FIG. 41 can also be called a vector modulator. In an embodiment, the "transmit" function performed by the WLAN interface/modem 3902 can be considered to be all processing performed by the WLAN interface/modem 3902 from receipt of baseband information through the LNA/PA 3904. An example implementation of the transmitter 3910 (vector modulator) is shown in FIGS. 57-60. The data conditioning interfaces 5802 in FIG. 58 effectively pre-process the I and Q signals 3942, 3944 before being received by the UFU modules 4102. An example BOM list for the transmitter 3910 of FIGS. 57-60 is shown in FIGS. 61A and 61B.

I and Q signals 3942, 3944 are received by UFU (universal frequency up-conversion) modules 4102A, 4102B. The UFU modules 4102A, 4102B each includes at least one UFT module 4104A, 4104B. The UFU modules 4102A, 4102B up-convert I and Q signals 3942, 3944. The UFU modules

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4102A, 4102B output up-converted I and Q signals 4106, 4108. The 90 degree combiner 4110 effectively phase shifts either the I signal 4106 or the Q signal 4108 by 90 degrees, and then combines the phase shifted signal with the unshifted signal to generate a combined, up-converted I/Q signal 3946.

In the example embodiment of FIG. 39, the modulation function is distributed among the transmitter 3910, the demodulator/modulator facilitation module 3912, and a baseband processor contained in the MAC interface 3914. The functions collectively performed by these components include, but are not limited to, differentially encoding data, splitting the baseband information signal into I and Q signals, scrambling data, and data spreading. The invention is not limited to this arrangement. These modulation-type functions can be centralized in a single component, or distributed in other ways.

An example implementation of the transmitter 3910 (vector modulator) is shown in FIGS. 57-60. The data conditioning interfaces 5802 in FIG. 58 effectively pre-process the I and Q signals 3942, 3944 before being received by the UFU modules 4102. An example BOM list for the transmitter 3910 of FIGS. 57-60 is shown in FIGS. 61A and 61B.

The components in the WLAN interface/modem 3902 are preferably controlled by the MAC interface 3914 in operation with the MAC 3918 in the computer 3916. This is represented by the distributed control arrow 3940 in FIG. 39. Such control includes setting the frequency, data rate, whether receiving or transmitting, and other communication characteristics/modes that will be apparent to persons skilled in the relevant art(s) based on the teachings contained herein. In embodiments, control signals are sent over the corresponding wireless medium and received by the antenna 3904, and sent to the MAC 3918.

FIG. 42 illustrates an example implementation of the WLAN interface/modem 3902. It is noted that in this implementation example, the MAC interface 3914 is located on a different board. FIG. 62 is an example motherboard corresponding to FIG. 42. FIG. 63 is an example bill-of-materials (BOM) list for the motherboard of FIG. 62. This and other implementations are provided herein for example purposes only. Other implementations will be apparent to persons skilled in the relevant art(s), and the invention is directed to such other implementations.

FIG. 102 illustrates an alternate example PCMCIA test bed assembly for a WLAN interface/modem 3902 according to an embodiment of the invention. In this embodiment, the baseband processor 10202 is separate from the MAC interface 3914.

In some applications, it is desired to separate the receive path and the transmit path. FIG. 43 illustrates an example receive implementation, and FIG. 44 illustrates an example transmit implementation.

## 7.2 Receiver

Example embodiments and implementations of the IQ receiver 3906 will be discussed as follows. The example embodiments and implementations include multi-phase embodiments that are useful for reducing or eliminating unwanted DC offsets and circuit re-radiation. The invention is not limited to these example receiver embodiments. Other receiver embodiments will be understood by those skilled in the relevant arts based on the discussion given herein. These other embodiments are within the scope and spirit of the present invention.



## 7.2.1 IQ Receiver

An example embodiment of the receiver 3906 is shown in FIG. 67A. Referring to FIG. 67A, the UFD module 4002A (FIG. 40) is configured so that the UFT module 4004A is coupled to a storage module 6704A. The UFT module 4004A is a controlled switch 6702A that is controlled by the control signal 3920A. The storage module 6704A is a capacitor 6706A. However, other storage modules could be used including an inductor, as will be understood by those skilled in the relevant arts. Likewise, the UFD module 4002B (FIG. 40) is configured so that the UFT module 4004B is coupled to a storage module 6704B. The UFT module 4004B is a controlled switch 6702B that is controlled by the control signal 3920B. The storage module 6704B is a capacitor 6706B. However, other storage modules could be used including an inductor, as will be understood by those skilled in the relevant arts. The operation of the receiver 3906 is discussed as follows.

The 90 degree splitter 4001 receives the received signal 3924 from the LNA/PA module 3904. The 90 degree splitter 4001 divides the signal 3924 into an I signal 4006A and a Q signal 4006B.

The UFD module 4002A receives the I signal 4006A and down-converts the I signal 4006A using the control signal 3920A to a lower frequency signal 13926. More specifically, the controlled switch 6702A samples the I signal 4006A according to the control signal 3920A, transferring charge (or energy) to the storage module 6704A. The charge stored during successive samples of the I signal 4006A, results in the down-converted signal I signal 3926. Likewise, UFD module 4002B receives the Q signal 4006B and down-converts the Q signal 4006B using the control signal 3920B to a lower frequency signal Q 3928. More specifically, the controlled switch 6702B samples the Q signal 4006B according to the control signal 3920B, resulting in charge (or energy) that is stored in the storage module 6704B. The charge stored during successive samples of the I signal 4006A, results in the down-converted signal Q signal 3928.

Down-conversion utilizing a UFD module (also called an aliasing module) is further described in the above referenced applications, such as "Method and System for Down-converting Electromagnetic Signals," Ser. No. 09/176,022, now U.S. Pat. No. 6,061,551. As discussed in the '551 patent, the control signals 3920A,B can be configured as a plurality of pulses that are established to improve energy transfer from the signals 4006A,B to the down-converted signals 3926 and 3928, respectively. In other words, the pulse widths of the control signals 3920 can be adjusted to increase and/or optimize the energy transfer from the signals 4006 to the down-converted output signals 3926 and 3928, respectively. Additionally, matched filter principles can be implemented to shape the sampling pulses of the control signal 3920, and therefore further improve energy transfer to the down-converted output signal 3106. Matched filter principle and energy transfer are further described in the above referenced applications, such as U.S. patent application titled, "Method and System for Down-Converting an Electromagnetic Signal, Transforms For Same, and Aperture Relationships", Ser. No. 09/550,644, filed on Apr. 14, 2000.

The configuration of the UFT based receiver 3906 is flexible. In FIG. 67A, the controlled switches 6702 are in a series configuration relative to the signals 4006. Alternatively, FIG. 67B illustrates the controlled switches 6702 in a shunt configuration so that the switches 6702 shunt the signals 4006 to ground.

Additionally in FIGS. 67A-B, the 90 degree phase shift between the I and Q channels is realized with the 90 degree

splitter 4001. Alternatively, FIG. 68A illustrates a receiver 6806 in series configuration, where the 90 degree phase shift is realized by shifting the control signal 3920B by 90 degrees relative to the control signal 3920A. More specifically, the 90 degree shifter 6804 is added to shift the control signal 3920B by 90 degrees relative to the control signal 3920A. As such, the splitter 6802 is an in-phase (i.e. 0 degree) signal splitter. FIG. 68B illustrates an embodiment of the receiver 3906 of the receiver 3906 in a shunt configuration with 90 degree delays on the control signal.

Furthermore, the configuration of the controlled switch 6702 is also flexible. More specifically, the controlled switches 6702 can be implemented in many different ways, including transistor switches. FIG. 69A illustrates the UFT modules 6702 in a series configuration and implemented as FETs 6902, where the gate of each FET 6902 is controlled by the respective control signal 3920. As such, the FET 6902 samples the respective signal 4006, according to the respective control signal 3920. FIG. 69B illustrates the shunt configuration.

## 7.2.2 Multi-Phase IQ Receiver

FIG. 70A illustrates an exemplary I/Q modulation receiver 7000, according to an embodiment of the present invention. I/Q modulation receiver 7000 has additional advantages of reducing or eliminating unwanted DC offsets and circuit re-radiation. As will be apparent, the IQ receiver 7000 can be described as a multi-phase receiver to those skilled in the arts.

I/Q modulation receiver 7000 comprises a first UFD module 7002, a first optional filter 7004, a second UFD module 7006, a second optional filter 7008, a third UFD module 7010, a third optional filter 7012, a fourth UFD module 7014, a fourth filter 7016, an optional LNA 7018, a first differential amplifier 7020, a second differential amplifier 7022, and an antenna 7072.

I/Q modulation receiver 7000 receives, down-converts, and demodulates a I/Q modulated RF input signal 7082 to an I baseband output signal 7084, and a Q baseband output signal 7086. I/Q modulated RF input signal 7082 comprises a first information signal and a second information signal that are I/Q modulated onto an RF carrier signal. I baseband output signal 7084 comprises the first baseband information signal. Q baseband output signal 7086 comprises the second baseband information signal.

Antenna 7072 receives I/Q modulated RF input signal 7082. I/Q modulated RF input signal 7082 is output by antenna 7072 and received by optional LNA 7018. When present, LNA 7018 amplifies I/Q modulated RF input signal 7082, and outputs amplified I/Q signal 7088.

First UFD module 7002 receives amplified I/Q signal 7088. First UFD module 7002 down-converts the I-phase signal portion of amplified input I/Q signal 7088 according to an I control signal 7090. First UFD module 7002 outputs an I output signal 7098.

In an embodiment, first UFD module 7002 comprises a first storage module 7024, a first UFT module 7026, and a first voltage reference 7028. In an embodiment, a switch contained within first UFT module 7026 opens and closes as a function of I control signal 7090. As a result of the opening and closing of this switch, which respectively couples and de-couples first storage module 7024 to and from first voltage reference 7028, a down-converted signal, referred to as I output signal 7098, results. First voltage reference 7028 may be any reference voltage, and is preferably ground. I output signal 7098 is stored by first storage module 7024.

In an embodiment, first storage module 7024 comprises a first capacitor 7074. In addition to storing I output signal

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7098, first capacitor 7074 reduces or prevents a DC offset voltage resulting from charge injection from appearing on I output signal 7098.

I output signal 7098 is received by optional first filter 7004. When present, first filter 7004 is in some embodiments a high pass filter to at least filter I output signal 7098 to remove any carrier signal "bleed through". In a preferred embodiment, when present, first filter 7004 comprises a first resistor 7030, a first filter capacitor 7032, and a first filter voltage reference 7034. Preferably, first resistor 7030 is coupled between I output signal 7098 and a filtered I output signal 7007, and first filter capacitor 7032 is coupled between filtered I output signal 7007 and first filter voltage reference 7034. Alternately, first filter 7004 may comprise any other applicable filter configuration as would be understood by persons skilled in the relevant art(s). First filter 7004 outputs filtered I output signal 7007.

Second UFD module 7006 receives amplified I/Q signal 7088. Second UFD module 7006 down-converts the inverted I-phase signal portion of amplified input I/Q signal 7088 according to an inverted I control signal 7092. Second UFD module 7006 outputs an inverted I output signal 7001.

In an embodiment, second UFD module 7006 comprises a second storage module 7036, a second UFT module 7038, and a second voltage reference 7040. In an embodiment, a switch contained within second UFT module 7038 opens and closes as a function of inverted I control signal 7092. As a result of the opening and closing of this switch, which respectively couples and de-couples second storage module 7036 to and from second voltage reference 7040, a down-converted signal, referred to as inverted I output signal 7001, results. Second voltage reference 7040 may be any reference voltage, and is preferably ground. Inverted I output signal 7001 is stored by second storage module 7036.

In an embodiment, second storage module 7036 comprises a second capacitor 7076. In addition to storing inverted I output signal 7001, second capacitor 7076 reduces or prevents a DC offset voltage resulting from charge injection from appearing on inverted I output signal 7001.

Inverted I output signal 7001 is received by optional second filter 7008. When present, second filter 7008 is a high pass filter to at least filter inverted I output signal 7001 to remove any carrier signal "bleed through". In a preferred embodiment, when present, second filter 7008 comprises a second resistor 7042, a second filter capacitor 7044, and a second filter voltage reference 7046. Preferably, second resistor 7042 is coupled between inverted I output signal 7001 and a filtered inverted I output signal 7009, and second filter capacitor 7044 is coupled between filtered inverted I output signal 7009 and second filter voltage reference 7046. Alternately, second filter 7008 may comprise any other applicable filter configuration as would be understood by persons skilled in the relevant art(s). Second filter 7008 outputs filtered inverted I output signal 7009.

First differential amplifier 7020 receives filtered I output signal 7007 at its non-inverting input and receives filtered inverted I output signal 7009 at its inverting input. First differential amplifier 7020 subtracts filtered inverted I output signal 7009 from filtered I output signal 7007, amplifies the result, and outputs I baseband output signal 7084. Because filtered inverted I output signal 7009 is substantially equal to an inverted version of filtered I output signal 7007, I baseband output signal 7084 is substantially equal to filtered I output signal 7009, with its amplitude doubled. Furthermore, filtered I output signal 7007 and filtered inverted I output signal 7009 may comprise substantially equal noise and DC offset contributions from prior down-conversion circuitry, including

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first UFD module 7002 and second UFD module 7006, respectively. When first differential amplifier 7020 subtracts filtered inverted I output signal 7009 from filtered I output signal 7007, these noise and DC offset contributions substantially cancel each other.

Third UFD module 7010 receives amplified I/Q signal 7088. Third UFD module 7010 down-converts the Q-phase signal portion of amplified input I/Q signal 7088 according to an Q control signal 7094. Third UFD module 7010 outputs an Q output signal 7003.

In an embodiment, third UFD module 7010 comprises a third storage module 7048, a third UFT module 7050, and a third voltage reference 7052. In an embodiment, a switch contained within third UFT module 7050 opens and closes as a function of Q control signal 7094. As a result of the opening and closing of this switch, which respectively couples and de-couples third storage module 7048 to and from third voltage reference 7052, a down-converted signal, referred to as Q output signal 7003, results. Third voltage reference 7052 may be any reference voltage, and is preferably ground. Q output signal 7003 is stored by third storage module 7048.

In an embodiment, third storage module 7048 comprises a third capacitor 7078. In addition to storing Q output signal 7003, third capacitor 7078 reduces or prevents a DC offset voltage resulting from charge injection from appearing on Q output signal 7003.

Q output signal 7003 is received by optional third filter 7012. When present, in an embodiment, third filter 7012 is a high pass filter to at least filter Q output signal 7003 to remove any carrier signal "bleed through". In an embodiment, when present, third filter 7012 comprises a third resistor 7054, a third filter capacitor 7056, and a third filter voltage reference 7058. Preferably, third resistor 7054 is coupled between Q output signal 7003 and a filtered Q output signal 7011, and third filter capacitor 7056 is coupled between filtered Q output signal 7011 and third filter voltage reference 7058. Alternately, third filter 7012 may comprise any other applicable filter configuration as would be understood by persons skilled in the relevant art(s). Third filter 7012 outputs filtered Q output signal 7011.

Fourth UFD module 7014 receives amplified I/Q signal 7088. Fourth UFD module 7014 down-converts the inverted Q-phase signal portion of amplified input I/Q signal 7088 according to an inverted Q control signal 7096. Fourth UFD module 7014 outputs an inverted Q output signal 7005.

In an embodiment, fourth UFD module 7014 comprises a fourth storage module 7060, a fourth UFT module 7062, and a fourth voltage reference 7064. In an embodiment, a switch contained within fourth UFT module 7062 opens and closes as a function of inverted Q control signal 7096. As a result of the opening and closing of this switch, which respectively couples and de-couples fourth storage module 7060 to and from fourth voltage reference 7064, a down-converted signal, referred to as inverted Q output signal 7005, results. Fourth voltage reference 7064 may be any reference voltage, and is preferably ground. Inverted Q output signal 7005 is stored by fourth storage module 7060.

In an embodiment, fourth storage module 7060 comprises a fourth capacitor 7080. In addition to storing inverted Q output signal 7005, fourth capacitor 7080 reduces or prevents a DC offset voltage resulting from charge injection from appearing on inverted Q output signal 7005.

Inverted Q output signal 7005 is received by optional fourth filter 7016. When present, fourth filter 7016 is a high pass filter to at least filter inverted Q output signal 7005 to remove any carrier signal "bleed through". In a preferred embodiment, when present, fourth filter 7016 comprises a

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fourth resistor **7066**, a fourth filter capacitor **7068**, and a fourth filter voltage reference **7070**. Preferably, fourth resistor **7066** is coupled between inverted Q output signal **7005** and a filtered inverted Q output signal **7013**, and fourth filter capacitor **7068** is coupled between filtered inverted Q output signal **7013** and fourth filter voltage reference **7070**. Alternatively, fourth filter **7016** may comprise any other applicable filter configuration as would be understood by persons skilled in the relevant art(s). Fourth filter **7016** outputs filtered inverted Q output signal **7013**.

Second differential amplifier **7022** receives filtered Q output signal **7011** at its non-inverting input and receives filtered inverted Q output signal **7013** at its inverting input. Second differential amplifier **7022** subtracts filtered inverted Q output signal **7013** from filtered Q output signal **7011**, amplifies the result, and outputs Q baseband output signal **7086**. Because filtered inverted Q output signal **7013** is substantially equal to an inverted version of filtered Q output signal **7011**, Q baseband output signal **7086** is substantially equal to filtered Q output signal **7013**, with its amplitude doubled. Furthermore, filtered Q output signal **7011** and filtered inverted Q output signal **7013** may comprise substantially equal noise and DC offset contributions of the same polarity from prior down-conversion circuitry, including third UFD module **7010** and fourth UFD module **7014**, respectively. When second differential amplifier **7022** subtracts filtered inverted Q output signal **7013** from filtered Q output signal **7011**, these noise and DC offset contributions substantially cancel each other.

Additional embodiments relating to addressing DC offset and re-radiation concerns, applicable to the present invention, are described in co-pending patent application Ser. No. 09/526,041, entitled "DC Offset, Re-radiation, and I/Q Solutions Using Universal Frequency Translation Technology," which is herein incorporated by reference in its entirety.

#### 7.2.2.1 Example I/Q Modulation Control Signal Generator Embodiments

FIG. **70B** illustrates an exemplary block diagram for I/Q modulation control signal generator **7023**, according to an embodiment of the present invention. I/Q modulation control signal generator **7023** generates I control signal **7090**, inverted I control signal **7092**, Q control signal **7094**, and inverted Q control signal **7096** used by I/Q modulation receiver **7000** of FIG. **70A**. I control signal **7090** and inverted I control signal **7092** operate to down-convert the I-phase portion of an input I/Q modulated RF signal. Q control signal **7094** and inverted Q control signal **7096** act to down-convert the Q-phase portion of the input I/Q modulated RF signal. Furthermore, I/Q modulation control signal generator **7023** has the advantage of generating control signals in a manner such that resulting collective circuit re-radiation is radiated at one or more frequencies outside of the frequency range of interest. For instance, potential circuit re-radiation is radiated at a frequency substantially greater than that of the input RF carrier signal frequency.

I/Q modulation control signal generator **7023** comprises a local oscillator **7025**, a first divide-by-two module **7027**, a 180 degree phase shifter **7029**, a second divide-by-two module **7031**, a first pulse generator **7033**, a second pulse generator **7035**, a third pulse generator **7037**, and a fourth pulse generator **7039**.

Local oscillator **7025** outputs an oscillating signal **7015**. FIG. **70C** shows an exemplary oscillating signal **7015**.

First divide-by-two module **7027** receives oscillating signal **7015**, divides oscillating signal **7015** by two, and outputs a half frequency LO signal **7017** and a half frequency inverted LO signal **7041**. FIG. **70C** shows an exemplary half frequency LO signal **7017**. Half frequency inverted LO signal **7041** is an

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inverted version of half frequency LO signal **7017**. First divide-by-two module **7027** may be implemented in circuit logic, hardware, software, or any combination thereof, as would be known by persons skilled in the relevant art(s).

180 degree phase shifter **7029** receives oscillating signal **7015**, shifts the phase of oscillating signal **7015** by 180 degrees, and outputs phase shifted LO signal **7019**. 180 degree phase shifter **7029** may be implemented in circuit logic, hardware, software, or any combination thereof, as would be known by persons skilled in the relevant art(s). In alternative embodiments, other amounts of phase shift may be used.

Second divide-by two module **7031** receives phase shifted LO signal **7019**, divides phase shifted LO signal **7019** by two, and outputs a half frequency phase shifted LO signal **7021** and a half frequency inverted phase shifted LO signal **7043**. FIG. **70C** shows an exemplary half frequency phase shifted LO signal **7021**. Half frequency inverted phase shifted LO signal **7043** is an inverted version of half frequency phase shifted LO signal **7021**. Second divide-by-two module **7031** may be implemented in circuit logic, hardware, software, or any combination thereof, as would be known by persons skilled in the relevant art(s).

First pulse generator **7033** receives half frequency LO signal **7017**, generates an output pulse whenever a rising edge is received on half frequency LO signal **7017**, and outputs I control signal **7090**. FIG. **70C** shows an exemplary I control signal **7090**.

Second pulse generator **7035** receives half frequency inverted LO signal **7041**, generates an output pulse whenever a rising edge is received on half frequency inverted LO signal **7041**, and outputs inverted I control signal **7092**. FIG. **70C** shows an exemplary inverted I control signal **7092**.

Third pulse generator **7037** receives half frequency phase shifted LO signal **7021**, generates an output pulse whenever a rising edge is received on half frequency phase shifted LO signal **7021**, and outputs Q control signal **7094**. FIG. **70C** shows an exemplary Q control signal **7094**.

Fourth pulse generator **7039** receives half frequency inverted phase shifted LO signal **7043**, generates an output pulse whenever a rising edge is received on half frequency inverted phase shifted LO signal **7043**, and outputs inverted Q control signal **7096**. FIG. **70C** shows an exemplary inverted Q control signal **7096**.

In an embodiment, control signals **7090**, **7021**, **7041** and **7043** include pulses having a width equal to one-half of a period of I/Q modulated RF input signal **7082**. The invention, however, is not limited to these pulse widths, and control signals **7090**, **7021**, **7041**, and **7043** may comprise pulse widths of any fraction of, or multiple and fraction of, a period of I/Q modulated RF input signal **7082**.

First, second, third, and fourth pulse generators **7033**, **7035**, **7037**, and **7039** may be implemented in circuit logic, hardware, software, or any combination thereof, as would be known by persons skilled in the relevant art(s).

As shown in FIG. **70C**, in an embodiment, control signals **7090**, **7021**, **7041**, and **7043** comprise pulses that are non-overlapping in other embodiments the pulses may overlap. Furthermore, in this example, pulses appear on these signals in the following order: I control signal **7090**, Q control signal **7094**, inverted I control signal **7092**, and inverted Q control signal **7096**. Potential circuit re-radiation from I/Q modulation receiver **7000** may comprise frequency components from a combination of these control signals.

For example, FIG. **70D** shows an overlay of pulses from I control signal **7090**, Q control signal **7094**, inverted I control signal **7092**, and inverted Q control signal **7096**. When pulses

from these control signals leak through first, second, third, and/or fourth UFD modules **7002**, **7006**, **7010**, and **7014** to antenna **7072** (shown in FIG. **70A**), they may be radiated from I/Q modulation receiver **7000**, with a combined waveform that appears to have a primary frequency equal to four times the frequency of any single one of control signals **7090**, **7021**, **7041**, and **7043**. FIG. **70** shows an example combined control signal **7045**.

FIG. **70D** also shows an example I/Q modulation RF input signal **7082** overlaid upon control signals **7090**, **7094**, **7092**, and **7096**. As shown in FIG. **70D**, pulses on I control signal **7090** overlay and act to down-convert a positive I-phase portion of I/Q modulation RF input signal **7082**. Pulses on inverted I control signal **7092** overlay and act to down-convert a negative I-phase portion of I/Q modulation RF input signal **7082**. Pulses on Q control signal **7094** overlay and act to down-convert a rising Q-phase portion of I/Q modulation RF input signal **7082**. Pulses on inverted Q control signal **7096** overlay and act to down-convert a falling Q-phase portion of I/Q modulation RF input signal **7082**.

As FIG. **70D** further shows in this example, the frequency ratio between the combination of control signals **7090**, **7021**, **7041**, and **7043** and I/Q modulation RF input signal **7082** is approximately 4:3. Because the frequency of the potentially re-radiated signal, i.e., combined control signal **7045**, is substantially different from that of the signal being down-converted, i.e., I/Q modulation RF input signal **7082**, it does not interfere with signal down-conversion as it is out of the frequency band of interest, and hence may be filtered out. In this manner, I/Q modulation receiver **7000** reduces problems due to circuit re-radiation. As will be understood by persons skilled in the relevant art(s) from the teachings herein, frequency ratios other than 4:3 may be implemented to achieve similar reduction of problems of circuit re-radiation.

It should be understood that the above control signal generator circuit example is provided for illustrative purposes only. The invention is not limited to these embodiments. Alternative embodiments (including equivalents, extensions, variations, deviations, etc., of the embodiments described herein) for I/Q modulation control signal generator **7023** will be apparent to persons skilled in the relevant art(s) from the teachings herein, and are within the scope of the present invention.

FIG. **70S** illustrates the receiver **7000**, where the UFT modules **7028**, **7038**, **7050**, and **7062** are configured with FETs **7099a-d**.

Additional embodiments relating to addressing DC offset and re-radiation concerns, applicable to the present invention, are described in co-pending patent application Ser. No. 09/526,041, entitled "DC Offset, Re-radiation, and I/Q Solutions Using Universal Frequency Translation Technology," which is herein incorporated by reference in its entirety.

#### 7.2.2.2 Implementation of Multi-phase I/Q Modulation Receiver Embodiment with Exemplary Waveforms

FIG. **70E** illustrates a more detailed example circuit implementation of I/Q modulation receiver **7000**, according to an embodiment of the present invention. FIGS. **70E-P** show example waveforms related to an example implementation of I/Q modulation receiver **7000** of FIG. **70E**.

FIGS. **70F** and **70G** show first and second input data signals **7047** and **7049** to be I/Q modulated with a RF carrier signal frequency as the I-phase and Q-phase information signals, respectively.

FIGS. **70I** and **70J** show the signals of FIGS. **70F** and **70G** after modulation with a RF carrier signal frequency, respectively, as I-modulated signal **7051** and Q-modulated signal **7053**.

FIG. **70H** shows an I/Q modulation RF input signal **7082** formed from I-modulated signal **7051** and Q-modulated signal **7053** of FIGS. **70I** and **70J**, respectively.

FIG. **70O** shows an overlaid view of filtered I output signal **7007** and filtered inverted I output signal **7009**.

FIG. **70P** shows an overlaid view of filtered Q output signal **7011** and filtered inverted Q output signal **7013**.

FIGS. **70K** and **70L** show I baseband output signal **7084** and Q baseband output signal **7086**, respectfully. A data transition **7055** is indicated in both I baseband output signal **7084** and Q baseband output signal **7086**. The corresponding data transition **7055** is indicated in I-modulated signal **7051** of FIG. **70I**, Q-modulated signal **7053** of FIG. **70J**, and I/Q modulation RF input signal **7082** of FIG. **70H**.

FIGS. **70M** and **70N** show I baseband output signal **7084** and Q baseband output signal **7086** over a wider time interval.

#### 7.2.2.3 Example Single Channel Receiver Embodiment

FIG. **70Q** illustrates an example single channel receiver **7091**, corresponding to either the I or Q channel of I/Q modulation receiver **7000**, according to an embodiment of the present invention. Single channel receiver **7091** can down-convert an input RF signal **7097** modulated according to AM, PM, FM, and other modulation schemes. Refer to section 7.2.1 above for further description on the operation of single channel receiver **7091**. In other words, the single channel receiver **7091** is a one channel of the IQ receiver **7000** that was discussed in section 7.2.1.

#### 7.2.2.4 Alternative Example I/Q Modulation Receiver Embodiment

FIG. **70R** illustrates an exemplary I/Q modulation receiver **7089**, according to an embodiment of the present invention. I/Q modulation receiver **7089** receives, down-converts, and demodulates an I/Q modulated RF input signal **7082** to an I baseband output signal **7084**, and a Q baseband output signal **7086**. I/Q modulation receiver **7089** has additional advantages of reducing or eliminating unwanted DC offsets and circuit re-radiation, in a similar fashion to that of I/Q modulation receiver **7000** described above.

### 7.3 Transmitter

Example embodiments and implementations of the IQ transmitter **3910** will be discussed as follows. The example embodiments and implementations include multi-phase embodiments that are useful for reducing or eliminating unwanted DC offsets that can result in unwanted carrier insertion.

#### 7.3.1 Universal Transmitter with 2 UFT Modules

FIG. **71A** illustrates a transmitter **7102** according to embodiments of the present invention. Transmitter **7102** includes a balanced modulator/up-converter **7104**, a control signal generator **7142**, an optional filter **7106**, and an optional amplifier **7108**. Transmitter **7102** up-converts a baseband signal **7110** to produce an output signal **7140** that is conditioned for wireless or wire line transmission. In doing so, the balanced modulator **7104** receives the baseband signal **7110** and samples the baseband signal in a differential and balanced fashion to generate a harmonically rich signal **7138**. The harmonically rich signal **7138** includes multiple harmonic images, where each image contains the baseband information in the baseband signal **7110**. The optional bandpass filter **7106** may be included to select a harmonic of interest (or a subset of harmonics) in the signal **7138** for transmission. The optional amplifier **7108** may be included to amplify the selected harmonic prior to transmission. The universal transmitter is further described at a high level by the flowchart

**8400** that is shown in FIG. **84**. A more detailed structural and operational description of the balanced modulator follows thereafter.

Referring to flowchart **8400**, in step **8402**, the balanced modulator **7104** receives the baseband signal **7110**.

In step **8404**, the balanced modulator **7104** samples the baseband signal in a differential and balanced fashion according to a first and second control signals that are phase shifted with respect to each other. The resulting harmonically rich signal **7138** includes multiple harmonic images that repeat at harmonics of the sampling frequency, where each image contains the necessary amplitude and frequency information to reconstruct the baseband signal **7110**.

In embodiments of the invention, the control signals include pulses having pulse widths (or apertures) that are established to improve energy transfer to a desired harmonic of the harmonically rich signal **7138**. In further embodiments of the invention, DC offset voltages are minimized between sampling modules as indicated in step **8406**, thereby minimizing carrier insertion in the harmonic images of the harmonically rich signal **7138**.

In step **8408**, the optional bandpass filter **7106** selects the desired harmonic of interest (or a subset of harmonics) in from the harmonically rich signal **7138** for transmission.

In step **8410**, the optional amplifier **7108** amplifies the selected harmonic(s) prior to transmission.

In step **8412**, the selected harmonic(s) is transmitted over a communications medium.

#### 7.3.1.1 Balanced Modulator Detailed Description

Referring to the example embodiment shown in FIG. **71A**, the balanced modulator **7104** includes the following components: a buffer/inverter **7112**; summer amplifiers **7118**, **7119**; UFT modules **7124** and **7128** having controlled switches **7148** and **7150**, respectively; an inductor **7126**; a blocking capacitor **7136**; and a DC terminal **7111**. As stated above, the balanced modulator **7104** differentially samples the baseband signal **7110** to generate a harmonically rich signal **7138**. More specifically, the UFT modules **7124** and **7128** sample the baseband signal in differential fashion according to control signals **7123** and **7127**, respectively. A DC reference voltage **7113** is applied to terminal **7111** and is uniformly distributed to the UFT modules **7124** and **7128**. The distributed DC voltage **7113** prevents any DC offset voltages from developing between the UFT modules, which can lead to carrier insertion in the harmonically rich signal **7138**. The operation of the balanced modulator **7104** is discussed in greater detail with reference to flowchart **8500** (FIG. **85**), as follows.

In step **8402**, the buffer/inverter **7112** receives the input baseband signal **7110** and generates input signal **7114** and inverted input signal **7116**. Input signal **7114** is substantially similar to signal **7110**, and inverted signal **7116** is an inverted version of signal **7114**. As such, the buffer/inverter **7112** converts the (single-ended) baseband signal **7110** into differential input signals **7114** and **7116** that will be sampled by the UFT modules. Buffer/inverter **7112** can be implemented using known operational amplifier (op amp) circuits, as will be understood by those skilled in the arts, although the invention is not limited to this example.

In step **8504**, the summer amplifier **7118** sums the DC reference voltage **7113** applied to terminal **7111** with the input signal **7114**, to generate a combined signal **7120**. Likewise, the summer amplifier **7119** sums the DC reference voltage **7113** with the inverted input signal **7116** to generate a combined signal **7122**. Summer amplifiers **7118** and **7119** can be implemented using known op amp summer circuits, and can be designed to have a specified gain or attenuation, including unity gain, although the invention is not limited to

this example. The DC reference voltage **7113** is also distributed to the outputs of both UFT modules **7124** and **7128** through the inductor **7126** as is shown.

In step **8506**, the control signal generator **7142** generates control signals **7123** and **7127** that are shown by way of example in FIG. **72B** and FIG. **72C**, respectively. As illustrated, both control signals **7123** and **7127** have the same period  $T_S$  as a master clock signal **7145** (FIG. **72A**), but have a pulse width (or aperture) of  $T_A$ . In the example, control signal **7123** triggers on the rising pulse edge of the master clock signal **7145**, and control signal **7127** triggers on the falling pulse edge of the master clock signal **7145**. Therefore, control signals **7123** and **7127** are shifted in time by 180 degrees relative to each other. In embodiments of invention, the master clock signal **7145** (and therefore the control signals **7123** and **7127**) have a frequency that is a sub-harmonic of the desired output signal **7140**. The invention is not limited to the example of FIGS. **72A-72C**.

In one embodiment, the control signal generator **7142** includes an oscillator **7146**, pulse generators **7144a** and **7144b**, and an inverter **7147** as shown. In operation, the oscillator **7146** generates the master clock signal **7145**, which is illustrated in FIG. **72A** as a periodic square wave having pulses with a period of  $T_S$ . Other clock signals could be used including but not limited to sinusoidal waves, as will be understood by those skilled in the arts. Pulse generator **7144a** receives the master clock signal **7145** and triggers on the rising pulse edge, to generate the control signal **7123**. Inverter **7147** inverts the clock signal **7145** to generate an inverted clock signal **7143**. The pulse generator **7144b** receives the inverted clock signal **7143** and triggers on the rising pulse edge (which is the falling edge of clock signal **7145**), to generate the control signal **7127**.

FIG. **89A-E** illustrate example embodiments for the pulse generator **7144**. FIG. **89A** illustrates a pulse generator **8902**. The pulse generator **8902** generates pulses **8908** having pulse width  $T_A$  from an input signal **8904**. Example input signals **8904** and pulses **8908** are depicted in FIGS. **89B** and **89C**, respectively. The input signal **8904** can be any type of periodic signal, including, but not limited to, a sinusoid, a square wave, a saw-tooth wave etc. The pulse width (or aperture)  $T_A$  of the pulses **8908** is determined by delay **8906** of the pulse generator **8902**. The pulse generator **8902** also includes an optional inverter **8910**, which is optionally added for polarity considerations as understood by those skilled in the arts. The example logic and implementation shown for the pulse generator **8902** is provided for illustrative purposes only, and is not limiting. The actual logic employed can take many forms. Additional examples of pulse generation logic are shown in FIGS. **89D** and **89E**. FIG. **89D** illustrates a rising edge pulse generator **8912** that triggers on the rising edge of input signal **8904**. FIG. **89E** illustrates a falling edge pulse generator **8916** that triggers on the falling edge of the input signal **8904**.

In step **8508**, the UFT module **7124** samples the combined signal **7120** according to the control signal **7123** to generate harmonically rich signal **7130**. More specifically, the switch **7148** closes during the pulse widths  $T_A$  of the control signal **7123** to sample the combined signal **7120** resulting in the harmonically rich signal **7130**. FIG. **71B** illustrates an exemplary frequency spectrum for the harmonically rich signal **7130** having harmonic images **7152a-n**. The images **7152** repeat at harmonics of the sampling frequency  $1/T_S$ , at infinity, where each image **7152** contains the necessary amplitude, frequency, and phase information to reconstruct the baseband signal **7110**. As discussed further below, the relative amplitude of the frequency images is generally a function of the harmonic number and the pulse width  $T_A$ . As such, the

relative amplitude of a particular harmonic **7152** can be increased (or decreased) by adjusting the pulse width  $T_A$  of the control signal **7123**. In general, shorter pulse widths of  $T_A$  shift more energy into the higher frequency harmonics, and longer pulse widths of  $T_A$  shift energy into the lower frequency harmonics. The generation of harmonically rich signals by sampling an input signal according to a controlled aperture have been described earlier in this application in the section titled, "Frequency Up-conversion Using Universal Frequency Translation", and is illustrated by FIGS. 3-6. A more detailed discussion of frequency up-conversion using a switch with a controlled sampling aperture is discussed in the co-pending patent application titled, "Method and System for Frequency Up-Conversion," Ser. No. 09/176,154, filed on Oct. 21, 1998, and incorporated herein by reference.

In step **8510**, the UFT module **7128** samples the combined signal **7122** according to the control signal **7127** to generate harmonically rich signal **7134**. More specifically, the switch **7150** closes during the pulse widths  $T_A$  of the control signal **7127** to sample the combined signal **7122** resulting in the harmonically rich signal **7134**. The harmonically rich signal **7134** includes multiple frequency images of baseband signal **7110** that repeat at harmonics of the sampling frequency ( $1/T_S$ ), similar to that for the harmonically rich signal **7130**. However, the images in the signal **7134** are phase-shifted compared to those in signal **7130** because of the inversion of signal **7116** compared to signal **7114**, and because of the relative phase shift between the control signals **7123** and **7127**.

In step **8512**, the node **7132** sums the harmonically rich signals **7130** and **7134** to generate harmonically rich signal **7133**. FIG. **71C** illustrates an exemplary frequency spectrum for the harmonically rich signal **7133** that has multiple images **7154a-n** that repeat at harmonics of the sampling frequency  $1/T_S$ . Each image **7154** includes the necessary amplitude, frequency and phase information to reconstruct the baseband signal **7110**. The capacitor **7136** operates as a DC blocking capacitor and substantially passes the harmonics in the harmonically rich signal **7133** to generate harmonically rich signal **7138** at the output of the modulator **7104**.

In step **8408**, the optional filter **7106** can be used to select a desired harmonic image for transmission. This is represented for example by a passband **7156** that selects the harmonic image **7154c** for transmission in FIG. **71C**.

An advantage of the modulator **7104** is that it is fully balanced, which substantially minimizes (or eliminates) any DC voltage offset between the two UFT modules **7124** and **7128**. DC offset is minimized because the reference voltage **7113** contributes a consistent DC component to the input signals **7120** and **7122** through the summing amplifiers **7118** and **7119**, respectively. Furthermore, the reference voltage **7113** is also directly coupled to the outputs of the UFT modules **7124** and **7128** through the inductor **7126** and the node **7132**. The result of controlling the DC offset between the UFT modules is that carrier insertion is minimized in the harmonic images of the harmonically rich signal **7138**. As discussed above, carrier insertion is substantially wasted energy because the information for a modulated signal is carried in the sidebands of the modulated signal and not in the carrier. Therefore, it is often desirable to minimize the energy at the carrier frequency by controlling the relative DC offset.

#### 7.3.1.2 Balanced Modulator Example Signal Diagrams and Mathematical Description

In order to further describe the invention, FIGS. **72D-72I** illustrate various example signal diagrams (vs. time) that are representative of the invention. These signal diagrams are meant for example purposes only and are not meant to be

limiting. FIG. **72D** illustrates a signal **7202** that is representative of the input baseband signal **7110** (FIG. **71A**). FIG. **72E** illustrates a step function **7204** that is an expanded portion of the signal **7202** from time  $t_0$  to  $t_1$ , and represents signal **7114** at the output of the buffer/inverter **7112**. Similarly, FIG. **72F** illustrates a signal **7206** that is an inverted version of the signal **7204**, and represents the signal **7116** at the inverted output of buffer/inverter **7112**. For analysis purposes, a step function is a good approximation for a portion of a single bit of data (for the baseband signal **7110**) because the clock rates of the control signals **7123** and **7127** are significantly higher than the data rates of the baseband signal **7110**. For example, if the data rate is in the KHz frequency range, then the clock rate will preferably be in MHz frequency range in order to generate an output signal in the GHz frequency range.

Still referring to FIGS. **72D-I**, FIG. **72G** illustrates a signal **7208** that is an example of the harmonically rich signal **7130** when the step function **7204** is sampled according to the control signal **7123** in FIG. **72B**. The signal **7208** includes positive pulses **7209** as referenced to the DC voltage **7113**. Likewise, FIG. **72H** illustrates a signal **7210** that is an example of the harmonically rich signal **7134** when the step function **7206** is sampled according to the control signal **7127**. The signal **7210** includes negative pulses **7211** as referenced to the DC voltage **7113**, which are time-shifted relative to the positive pulses **7209** in signal **7208**.

Still referring to FIGS. **72D-I**, the FIG. **72I** illustrates a signal **7212** that is the combination of signal **7208** (FIG. **72G**) and the signal **7210** (FIG. **72H**), and is an example of the harmonically rich signal **7133** at the output of the summing node **7132**. As illustrated, the signal **7212** spends approximately as much time above the DC reference voltage **7113** as below the DC reference voltage **7113** over a limited time period. For example, over a time period **7214**, the energy in the positive pulses **7209a-b** is canceled out by the energy in the negative pulses **7211a-b**. This is indicative of minimal (or zero) DC offset between the UFT modules **7124** and **7128**, which results in minimal carrier insertion during the sampling process.

Still referring to FIG. **72I**, the time axis of the signal **7212** can be phased in such a manner to represent the waveform as an odd function. For such an arrangement, the Fourier series is readily calculated to obtain:

$$I_c(t) = \sum_{n=1}^{\infty} \left( \frac{4 \sin\left(\frac{n\pi T_A}{T_S}\right) \cdot \sin\left(\frac{n\pi}{2}\right)}{n\pi} \right) \cdot \sin\left(\frac{2n\pi t}{T_S}\right). \quad \text{Equation 1}$$

where:

$T_S$ =period of the master clock **7145**

$T_A$ =pulse width of the control signals **7123** and **7127**

$n$ =harmonic number

As shown by Equation 1, the relative amplitude of the frequency images is generally a function of the harmonic number  $n$ , and the ratio of  $T_A/T_S$ . As indicated, the  $T_A/T_S$  ratio represents the ratio of the pulse width of the control signals relative to the period of the sub-harmonic master clock. The  $T_A/T_S$  ratio can be optimized in order to maximize the amplitude of the frequency image at a given harmonic. For example, if a passband waveform is desired to be created at  $5\times$  the frequency of the sub-harmonic clock, then a baseline power for that harmonic extraction may be calculated for the fifth harmonic ( $n=5$ ) as:

$$I_c(t) = \left( \frac{4 \sin\left(\frac{5\pi T_A}{T_S}\right)}{5\pi} \right) \cdot \sin(5\omega_s t).$$

Equation 2

As shown by Equation 2,  $I_c(t)$  for the fifth harmonic is a sinusoidal function having an amplitude that is proportional to the  $\sin(5\pi T_A/T_S)$ . The signal amplitude can be maximized by setting  $T_A = (1/10) \cdot T_S$  so that  $\sin(5\pi T_A/T_S) = \sin(\pi/2) = 1$ . Doing so results in the equation:

$$I_c(t) |_{n=5} = \frac{4}{5\pi} (\sin(5\omega_s t)).$$

Equation 3

This component is a frequency at  $5\times$  of the sampling frequency of sub-harmonic clock, and can be extracted from the Fourier series via a bandpass filter (such as bandpass filter **7106**) that is centered around  $5f_s$ . The extracted frequency component can then be optionally amplified by the amplifier **7108** prior to transmission on a wireless or wire-line communications channel or channels.

Equation 3 can be extended to reflect the inclusion of a message signal as illustrated by equation 4 below:

$$m(t) \cdot I_c(t) \Big|_{\substack{n=5 \\ \theta=\theta(t)}} = \frac{4 \cdot m(t)}{5\pi} (\sin(5\omega_s t + 5\theta(t))).$$

Equation 4

Equation 4 illustrates that a message signal can be carried in harmonically rich signals **7133** such that both amplitude and phase can be modulated. In other words,  $m(t)$  is modulated for amplitude and  $\theta(t)$  is modulated for phase. In such cases, it should be noted that  $\theta(t)$  is augmented modulo  $n$  while the amplitude modulation  $m(t)$  is simply scaled. Therefore, complex waveforms may be reconstructed from their Fourier series with multiple aperture UFT combinations.

As discussed above, the signal amplitude for the 5th harmonic was maximized by setting the sampling aperture width  $T_A = 1/10 T_S$ , where  $T_S$  is the period of the master clock signal. This can be restated and generalized as setting  $T_A = 1/2$  the period (or  $\pi$  radians) at the harmonic of interest. In other words, the signal amplitude of any harmonic  $n$  can be maximized by sampling the input waveform with a sampling aperture of  $T_A = 1/2$  the period of the harmonic of interest ( $n$ ). Based on this discussion, it is apparent that varying the aperture changes the harmonic and amplitude content of the output waveform. For example, if the sub-harmonic clock has a frequency of 200 MHz, then the fifth harmonic is at 1 GHz. The amplitude of the fifth harmonic is maximized by setting the aperture width  $T_A = 500$  picoseconds, which equates to  $1/2$  the period (or  $\pi$  radians) at 1 GHz.

FIG. **72J** depicts a frequency plot **7216** that graphically illustrates the effect of varying the sampling aperture of the control signals on the harmonically rich signal **7133** given a 200 MHz harmonic clock. The frequency plot **7216** compares two frequency spectrums **7218** and **7220** for different control signal apertures given a 200 MHz clock. More specifically, the frequency spectrum **7218** is an example spectrum for signal **7133** given the 200 MHz clock with the aperture  $T_A = 500$  psec (where 500 psec is  $\pi$  radians at the 5th harmonic of 1 GHz). Similarly, the frequency spectrum **7220** is an example spectrum for signal **7133** given a 200 MHz clock that is a square wave (so  $T_A = 5000$  psec). The spectrum **7218** includes multiple harmonics **7218a-I**, and the frequency

spectrum **7220** includes multiple harmonics **7220a-e**. [It is noted that spectrum **7220** includes only the odd harmonics as predicted by Fourier analysis for a square wave.] At 1 GHz (which is the 5th harmonic), the signal amplitude of the two frequency spectrums **7218e** and **7220c** are approximately equal. However, at 200 MHz, the frequency spectrum **7218a** has a much lower amplitude than the frequency spectrum **7220a**, and therefore the frequency spectrum **7218** is more efficient than the frequency spectrum **7220**, assuming the desired harmonic is the 5th harmonic. In other words, assuming 1 GHz is the desired harmonic, the frequency spectrum **7218** wastes less energy at the 200 MHz fundamental than does the frequency spectrum **7218**.

### 7.3.1.3 Balanced Modulator Having a Shunt Configuration

FIG. **79A** illustrates a universal transmitter **7900** that is a second embodiment of a universal transmitter having two balanced UFT modules in a shunt configuration. (In contrast, the balanced modulator **7104** can be described as having a series configuration based on the orientation of the UFT modules.) Transmitter **7900** includes a balanced modulator **7901**, the control signal generator **7142**, the optional bandpass filter **7106**, and the optional amplifier **7108**. The transmitter **7900** up-converts a baseband signal **7902** to produce an output signal **7936** that is conditioned for wireless or wire line transmission. In doing so, the balanced modulator **7901** receives the baseband signal **7902** and shunts the baseband signal to ground in a differential and balanced fashion to generate a harmonically rich signal **7934**. The harmonically rich signal **7934** includes multiple harmonic images, where each image contains the baseband information in the baseband signal **7902**. In other words, each harmonic image includes the necessary amplitude, frequency, and phase information to reconstruct the baseband signal **7902**. The optional bandpass filter **7106** may be included to select a harmonic of interest (or a subset of harmonics) in the signal **7934** for transmission. The optional amplifier **7108** may be included to amplify the selected harmonic prior to transmission, resulting in the output signal **7936**.

The balanced modulator **7901** includes the following components: a buffer/inverter **7904**; optional impedances **7910**, **7912**; UFT modules **7916** and **7922** having controlled switches **7918** and **7924**, respectively; blocking capacitors **7928** and **7930**; and a terminal **7920** that is tied to ground. As stated above, the balanced modulator **7901** differentially shunts the baseband signal **7902** to ground, resulting in a harmonically rich signal **7934**. More specifically, the UFT modules **7916** and **7922** alternately shunts the baseband signal to terminal **7920** according to control signals **7123** and **7127**, respectively. Terminal **7920** is tied to ground and prevents any DC offset voltages from developing between the UFT modules **7916** and **7922**. As described above, a DC offset voltage can lead to undesired carrier insertion. The operation of the balanced modulator **7901** is described in greater detail according to the flowchart **8600** (FIG. **86**) as follows.

In step **8402**, the buffer/inverter **7904** receives the input baseband signal **7902** and generates I signal **7906** and inverted I signal **7908**. I signal **7906** is substantially similar to the baseband signal **7902**, and the inverted I signal **7908** is an inverted version of signal **7902**. As such, the buffer/inverter **7904** converts the (single-ended) baseband signal **7902** into differential signals **7906** and **7908** that are sampled by the UFT modules. Buffer/inverter **7904** can be implemented using known operational amplifier (op amp) circuits, as will be understood by those skilled in the arts, although the invention is not limited to this example.



In step 8604, the control signal generator 7142 generates control signals 7123 and 7127 from the master clock signal 7145. Examples of the master clock signal 7145, control signal 7123, and control signal 7127 are shown in FIGS. 72A-C, respectively. As illustrated, both control signals 7123 and 7127 have the same period  $T_S$  as a master clock signal 7145, but have a pulse width (or aperture) of  $T_A$ . Control signal 7123 triggers on the rising pulse edge of the master clock signal 7145, and control signal 7127 triggers on the falling pulse edge of the master clock signal 7145. Therefore, control signals 7123 and 7127 are shifted in time by 180 degrees relative to each other. A specific embodiment of the control signal generator 7142 is illustrated in FIG. 71A, and was discussed in detail above.

In step 8606, the UFT module 7916 shunts the signal 7906 to ground according to the control signal 7123, to generate a harmonically rich signal 7914. More specifically, the switch 7918 closes and shorts the signal 7906 to ground (at terminal 7920) during the aperture width  $T_A$  of the control signal 7123, to generate the harmonically rich signal 7914. FIG. 79B illustrates an exemplary frequency spectrum for the harmonically rich signal 7918 having harmonic images 7950a-n. The images 7950 repeat at harmonics of the sampling frequency  $1/T_S$ , at infinitum, where each image 7950 contains the necessary amplitude, frequency, and phase information to reconstruct the baseband signal 7902. The generation of harmonically rich signals by sampling an input signal according to a controlled aperture have been described earlier in this application in the section titled, "Frequency Up-conversion Using Universal Frequency Translation", and is illustrated by FIGS. 3-6. A more detailed discussion of frequency up-conversion using a switch with a controlled sampling aperture is discussed in the co-pending patent application titled, "Method and System for Frequency Up-Conversion," Ser. No. 09/176,154, filed on Oct. 21, 1998, and incorporated herein by reference.

The relative amplitude of the frequency images 7950 are generally a function of the harmonic number and the pulse width  $T_A$ . As such, the relative amplitude of a particular harmonic 7950 can be increased (or decreased) by adjusting the pulse width  $T_A$  of the control signal 7123. In general, shorter pulse widths of  $T_A$  shift more energy into the higher frequency harmonics, and longer pulse widths of  $T_A$  shift energy into the lower frequency harmonics, as described by equations 1-4 above. Additionally, the relative amplitude of a particular harmonic 7950 can also be adjusted by adding/tuning an optional impedance 7910. Impedance 7910 operates as a filter that emphasizes a particular harmonic in the harmonically rich signal 7914.

In step 8608, the UFT module 7922 shunts the inverted signal 7908 to ground according to the control signal 7127, to generate a harmonically rich signal 7926. More specifically, the switch 7924 closes during the pulse widths  $T_A$  and shorts the inverted I signal 7908 to ground (at terminal 7920), to generate the harmonically rich signal 7926. At any given time, only one of input signals 7906 or 7908 is shorted to ground because the pulses in the control signals 7123 and 7127 are phase shifted with respect to each other, as shown in FIGS. 72B and 72C.

The harmonically rich signal 7926 includes multiple frequency images of baseband signal 7902 that repeat at harmonics of the sampling frequency ( $1/T_S$ ), similar to that for the harmonically rich signal 7914. However, the images in the signal 7926 are phase-shifted compared to those in signal 7914 because of the inversion of the signal 7908 compared to the signal 7906, and because of the relative phase shift between the control signals 7123 and 7127. The optional

impedance 7912 can be included to emphasize a particular harmonic of interest, and is similar to the impedance 7910 above.

In step 8610, the node 7932 sums the harmonically rich signals 7914 and 7926 to generate the harmonically rich signal 7934. The capacitors 7928 and 7930 operate as blocking capacitors that substantially pass the respective harmonically rich signals 7914 and 7926 to the node 7932. (The capacitor values may be chosen to substantially block baseband frequency components as well.) FIG. 79C illustrates an exemplary frequency spectrum for the harmonically rich signal 7934 that has multiple images 7952a-n that repeat at harmonics of the sampling frequency  $1/T_S$ . Each image 7952 includes the necessary amplitude, frequency, and phase information to reconstruct the baseband signal 7902. The optional filter 7106 can be used to select the harmonic image of interest for transmission. This is represented by a passband 7956 that selects the harmonic image 7932c for transmission.

An advantage of the modulator 7901 is that it is fully balanced, which substantially minimizes (or eliminates) any DC voltage offset between the two UFT modules 7912 and 7914. DC offset is minimized because the UFT modules 7916 and 7922 are both connected to ground at terminal 7920. The result of controlling the DC offset between the UFT modules is that carrier insertion is minimized in the harmonic images of the harmonically rich signal 7934. As discussed above, carrier insertion is substantially wasted energy because the information for a modulated signal is carried in the sidebands of the modulated signal and not in the carrier. Therefore, it is often desirable to minimize the energy at the carrier frequency by controlling the relative DC offset.

#### 7.3.1.4 Balanced Modulator FET Configuration

As described above, the balanced modulators 7104 and 7901 utilize two balanced UFT modules to sample the input baseband signals to generate harmonically rich signals that contain the up-converted baseband information. More specifically, the UFT modules include controlled switches that sample the baseband signal in a balanced and differential fashion. FIGS. 71D and 79D illustrate embodiments of the controlled switch in the UFT module.

FIG. 71D illustrates an example embodiment of the modulator 7104 (FIG. 71B) where the controlled switches in the UFT modules are field effect transistors (FET). More specifically, the controlled switches 7148 and 7128 are embodied as FET 7158 and FET 7160, respectively. The FET 7158 and 7160 are oriented so that their gates are controlled by the control signals 7123 and 7127, so that the control signals control the FET conductance. For the FET 7158, the combined baseband signal 7120 is received at the source of the FET 7158 and is sampled according to the control signal 7123 to produce the harmonically rich signal 7130 at the drain of the FET 7158. Likewise, the combined baseband signal 7122 is received at the source of the FET 7160 and is sampled according to the control signal 7127 to produce the harmonically rich signal 7134 at the drain of FET 7160. The source and drain orientation that is illustrated is not limiting, as the source and drains can be switched for most FETs. In other words, the combined baseband signal can be received at the drain of the FETs, and the harmonically rich signals can be taken from the source of the FETs, as will be understood by those skilled in the relevant arts.

FIG. 79D illustrates an embodiment of the modulator 7900 (FIG. 79A) where the controlled switches in the UFT modules are field effect transistors (FET). More specifically, the controlled switches 7918 and 7924 are embodied as FET 7936 and FET 7938, respectively. The FETs 7936 and 7938 are oriented so that their gates are controlled by the control



signals **7123** and **7127**, respectively, so that the control signals determine FET conductance. For the FET **7936**, the baseband signal **7906** is received at the source of the FET **7936** and shunted to ground according to the control signal **7123**, to produce the harmonically rich signal **7914**. Likewise, the baseband signal **7908** is received at the source of the FET **7938** and is shunted to grounding according to the control signal **7127**, to produce the harmonically rich signal **7926**. The source and drain orientation that is illustrated is not limiting, as the source and drains can be switched for most FETs, as will be understood by those skilled in the relevant arts.

### 7.3.1.5 Universal Transmitter Configured for Carrier Insertion

As discussed above, the transmitters **7102** and **7900** have a balanced configuration that substantially eliminates any DC offset and results in minimal carrier insertion in the output signal **7140**. Minimal carrier insertion is generally desired for most applications because the carrier signal carries no information and reduces the overall transmitter efficiency. However, some applications require the received signal to have sufficient carrier energy for the receiver to extract the carrier for coherent demodulation. In support thereof, the present invention can be configured to provide the necessary carrier insertion by implementing a DC offset between the two sampling UFT modules.

FIG. **73A** illustrates a transmitter **7302** that up-converts a baseband signal **7306** to an output signal **7322** having carrier insertion. As is shown, the transmitter **7302** is similar to the transmitter **7102** (FIG. **71A**) with the exception that the up-converter/modulator **7304** is configured to accept two DC reference voltages. In contrast, modulator **7104** was configured to accept only one DC reference voltage. More specifically, the modulator **7304** includes a terminal **7309** to accept a DC reference voltage **7308**, and a terminal **7313** to accept a DC reference voltage **7314**.  $V_r$  **7308** appears at the UFT module **7124** through summer amplifier **7118** and the inductor **7310**.  $V_r$  **7314** appears at UFT module **7128** through the summer amplifier **7119** and the inductor **7316**. Capacitors **7312** and **7318** operate as blocking capacitors. If  $V_r$  **7308** is different from  $V_r$  **7314** then a DC offset voltage will exist between UFT module **7124** and UFT module **7128**, which will be up-converted at the carrier frequency in the harmonically rich signal **7320**. More specifically, each harmonic image in the harmonically rich signal **7320** will include a carrier signal as depicted in FIG. **73B**.

FIG. **73B** illustrates an exemplary frequency spectrum for the harmonically rich signal **7320** that has multiple harmonic images **7324a-n**. In addition to carrying the baseband information in the sidebands, each harmonic image **7324** also includes a carrier signal **7326** that exists at respective harmonic of the sampling frequency  $1/T_s$ . The amplitude of the carrier signal increases with increasing DC offset voltage. Therefore, as the difference between  $V_r$  **7308** and  $V_r$  **7314** widens, the amplitude of each carrier signal **7326** increases. Likewise, as the difference between  $V_r$  **7308** and  $V_r$  **7314** shrinks, the amplitude of each carrier signal **7326** shrinks. As with transmitter **7302**, the optional bandpass filter **7106** can be included to select a desired harmonic image for transmission. This is represented by passband **7328** in FIG. **73B**.

### 7.3.2 Universal Transmitter in I Q Configuration:

As described above, the balanced modulators **7104** and **7901** up-convert a baseband signal to a harmonically rich signal having multiple harmonic images of the baseband information. By combining two balanced modulators, IQ configurations can be formed for up-converting I and Q baseband signals. In doing so, either the (series type) balanced

modulator **7104** or the (shunt type) balanced modulator **7901** can be utilized. IQ modulators having both series and shunt configurations are described below.

### 7.3.2.1 IQ Transmitter Using Series-Type Balanced Modulator

FIG. **74** illustrates an IQ transmitter **7420** with an in-phase (I) and quadrature (Q) configuration according to embodiments of the invention. The transmitter **7420** includes an IQ balanced modulator **7410**, an optional filter **7414**, and an optional amplifier **7416**. The transmitter **7420** is useful for transmitting complex I Q waveforms and does so in a balanced manner to control DC offset and carrier insertion. In doing so, the modulator **7410** receives an I baseband signal **7402** and a Q baseband signal **7404** and up-converts these signals to generate a combined harmonically rich signal **7412**. The harmonically rich signal **7412** includes multiple harmonics images, where each image contains the baseband information in the I signal **7402** and the Q signal **7404**. The optional bandpass filter **7414** may be included to select a harmonic of interest (or subset of harmonics) from the signal **7412** for transmission. The optional amplifier **7416** may be included to amplify the selected harmonic prior to transmission, to generate the IQ output signal **7418**.

As stated above, the balanced IQ modulator **7410** up-converts the I baseband signal **7402** and the Q baseband signal **7404** in a balanced manner to generate the combined harmonically rich signal **7412** that carries the I and Q baseband information. To do so, the modulator **7410** utilizes two balanced modulators **7104** from FIG. **71A**, a signal combiner **7408**, and a DC terminal **7407**. The operation of the balanced modulator **7410** and other circuits in the transmitter is described according to the flowchart **8700** in FIG. **87**, as follows.

In step **8702**, the IQ modulator **7410** receives the I baseband signal **7402** and the Q baseband signal **7404**.

In step **8704**, the I balanced modulator **7104a** samples the I baseband signal **7402** in a differential fashion using the control signals **7123** and **7127** to generate a harmonically rich signal **7411a**. The harmonically rich signal **7411a** contains multiple harmonic images of the I baseband information, similar to the harmonically rich signal **7130** in FIG. **71B**.

In step **8706**, the balanced modulator **7104b** samples the Q baseband signal **7404** in a differential fashion using control signals **7123** and **7127** to generate harmonically rich signal **7411b**, where the harmonically rich signal **7411b** contains multiple harmonic images of the Q baseband signal **7404**. The operation of the balanced modulator **7104** and the generation of harmonically rich signals was fully described above and illustrated in FIGS. **71A-C**, to which the reader is referred for further details.

In step **8708**, the DC terminal **7407** receives a DC voltage **7406** that is distributed to both modulators **7104a** and **7104b**. The DC voltage **7406** is distributed to both the input and output of both UFT modules **7124** and **7128** in each modulator **7104**. This minimizes (or prevents) DC offset voltages from developing between the four UFT modules, and thereby minimizes or prevents any carrier insertion during the sampling steps **8704** and **8706**.

In step **8710**, the 90 degree signal combiner **7408** combines the harmonically rich signals **7411a** and **7411b** to generate IQ harmonically rich signal **7412**. This is further illustrated in FIGS. **75A-C**. FIG. **75A** depicts an exemplary frequency spectrum for the harmonically rich signal **7411a** having harmonic images **7502a-n**. The images **7502** repeat at harmonics of the sampling frequency  $1/T_s$ , where each image **7502** contains the necessary amplitude and frequency information to reconstruct the I baseband signal **7402**. Likewise, FIG. **75B**

depicts an exemplary frequency spectrum for the harmonically rich signal **7411b** having harmonic images **7504a-n**. The harmonic images **7504a-n** also repeat at harmonics of the sampling frequency  $1/T_s$ , where each image **7504** contains the necessary amplitude, frequency, and phase information to reconstruct the Q baseband signal **7404**. FIG. 75C illustrates an exemplary frequency spectrum for the combined harmonically rich signal **7412** having images **7506**. Each image **7506** carries the I baseband information and the Q baseband information from the corresponding images **7502** and **7504**, respectively, without substantially increasing the frequency bandwidth occupied by each harmonic **7506**. This can occur because the signal combiner **7408** phase shifts the Q signal **7411b** by 90 degrees relative to the I signal **7411a**. The result is that the images **7502a-n** and **7504a-n** effectively share the signal bandwidth do to their orthogonal relationship. For example, the images **7502a** and **7504a** effectively share the frequency spectrum that is represented by the image **7506a**.

In step **8712**, the optional filter **7414** can be included to select a harmonic of interest, as represented by the passband **7508** selecting the image **7506c** in FIG. 75c.

In step **8714**, the optional amplifier **7416** can be included to amplify the harmonic (or harmonics) of interest prior to transmission.

In step **8716**, the selected harmonic (or harmonics) is transmitted over a communications medium.

FIG. 76A illustrates a transmitter **7608** that is a second embodiment for an I Q transmitter having a balanced configuration. Transmitter **7608** is similar to the transmitter **7420** except that the 90 degree phase shift between the I and Q channels is achieved by phase shifting the control signals instead of using a 90 degree signal combiner to combine the harmonically rich signals. More specifically, delays **7604a** and **7604b** delay the control signals **7123** and **7127** for the Q channel modulator **7104b** by 90 degrees relative to the control signals for the I channel modulator **7104a**. As a result, the Q modulator **7104b** samples the Q baseband signal **7404** with 90 degree delay relative to the sampling of the I baseband signal **7402** by the I channel modulator **7104a**. Therefore, the Q harmonically rich signal **7411b** is phase shifted by 90 degrees relative to the I harmonically rich signal. Since the phase shift is achieved using the control signals, an in-phase signal combiner **7606** combines the harmonically rich signals **7411a** and **7411b**, to generate the harmonically rich signal **7412**.

FIG. 76B illustrates a transmitter **7618** that is similar to transmitter **7608** in FIG. 76A. The difference being that the transmitter **7618** has a modulator **7620** that utilizes a summing node **7622** to sum the signals **7411a** and **7411b** instead of the in-phase signal combiner **7606** that is used in modulator **7602** of transmitter **7608**.

FIG. 90A-90D illustrate various detailed circuit implementations of the transmitter **7420** in FIG. 74. These circuit implementations are meant for example purposes only, and are not meant to be limiting.

FIG. 90A illustrates I input circuitry **9002a** and Q input circuitry **9002b** that receive the I and Q input signals **7402** and **7404**, respectively.

FIG. 90B illustrates the I channel circuitry **9006** that processes an I data **9004a** from the I input circuit **9002a**.

FIG. 90C illustrates the Q channel circuitry **9008** that processes the Q data **9004b** from the Q input circuit **9002b**.

FIG. 90D illustrates the output combiner circuit **9012** that combines the I channel data **9007** and the Q channel data **9010** to generate the output signal **7418**.

### 7.3.2.2 IQ Transmitter Using Shunt-Type Balanced Modulator

FIG. 80 illustrates an IQ transmitter **8000** that is another IQ transmitter embodiment according to the present invention. The transmitter **8000** includes an IQ balanced modulator **8001**, an optional filter **8012**, and an optional amplifier **8014**. During operation, the modulator **8001** up-converts an I baseband signal **8002** and a Q baseband signal **8004** to generate a combined harmonically rich signal **8011**. The harmonically rich signal **8011** includes multiple harmonics images, where each image contains the baseband information in the I signal **8002** and the Q signal **8004**. The optional bandpass filter **8012** may be included to select a harmonic of interest (or subset of harmonics) from the harmonically rich signal **8011** for transmission. The optional amplifier **8014** may be included to amplify the selected harmonic prior to transmission, to generate the IQ output signal **8016**.

The IQ modulator **8001** includes two shunt balanced modulators **7901** from FIG. 79A, and a 90 degree signal combiner **8010** as shown. The operation of the IQ modulator **8001** is described in reference to the flowchart **8800** (FIG. 88), as follows. The order of the steps in flowchart **8800** is not limiting.

In step **8802**, the balanced modulator **8001** receives the I baseband signal **8002** and the Q baseband signal **8004**.

In step **8804**, the balanced modulator **7901a** differentially shunts the I baseband signal **8002** to ground according to the control signals **7123** and **7127**, to generate a harmonically rich signal **8006**. More specifically, the UFT modules **7916a** and **7922a** alternately shunt the I baseband signal **8002** and an inverted version of the I baseband signal **8002** to ground according to the control signals **7123** and **7127**, respectively. The operation of the balanced modulator **7901** and the generation of harmonically rich signals was fully described above and is illustrated in FIGS. 79A-C, to which the reader is referred for further details. As such, the harmonically rich signal **8006** contains multiple harmonic images of the I baseband information as described above.

In step **8806**, the balanced modulator **7901b** differentially shunts the Q baseband signal **8004** to ground according to control signals **7123** and **7127**, to generate harmonically rich signal **8008**. More specifically, the UFT modules **7916b** and **7922b** alternately shunt the Q baseband signal **8004** and an inverted version of the Q baseband signal **8004** to ground, according to the control signals **7123** and **7127**, respectively. As such, the harmonically rich signal **8008** contains multiple harmonic images that contain the Q baseband information.

In step **8808**, the 90 degree signal combiner **8010** combines the harmonically rich signals **8006** and **8008** to generate IQ harmonically rich signal **8011**. This is further illustrated in FIGS. 81A-C. FIG. 81A depicts an exemplary frequency spectrum for the harmonically rich signal **8006** having harmonic images **8102a-n**. The harmonic images **8102a-n** repeat at harmonics of the sampling frequency  $1/T_s$ , where each image **8102** contains the necessary amplitude, frequency, and phase information to reconstruct the I baseband signal **8002**. Likewise, FIG. 81B depicts an exemplary frequency spectrum for the harmonically rich signal **8008** having harmonic images **8104a-n**. The harmonic images **8104a-n** also repeat at harmonics of the sampling frequency  $1/T_s$ , where each image **8104** contains the necessary amplitude, frequency, and phase information to reconstruct the Q baseband signal **8004**. FIG. 81C illustrates an exemplary frequency spectrum for the IQ harmonically rich signal **8011** having images **8106a-n**. Each image **8106** carries the I baseband information and the Q baseband information from the corresponding images **8102** and **8104**, respectively, without substantially increasing the frequency bandwidth occupied by each image **8106**. This can

occur because the signal combiner **8010** phase shifts the Q signal **8008** by 90 degrees relative to the I signal **8006**.

In step **8810**, the optional filter **8012** may be included to select a harmonic of interest, as represented by the passband **8108** selecting the image **8106c** in FIG. **81C**.

In step **8812**, the optional amplifier **8014** can be included to amplify the selected harmonic image **8106** prior to transmission.

In step **8814**, the selected harmonic (or harmonics) is transmitted over a communications medium.

FIG. **82** illustrates a transmitter **8200** that is another embodiment for an IQ transmitter having a balanced configuration. Transmitter **8200** is similar to the transmitter **8000** except that the 90 degree phase shift between the I and Q channels is achieved by phase shifting the control signals instead of using a 90 degree signal combiner to combine the harmonically rich signals. More specifically, delays **8204a** and **8204b** delay the control signals **7123** and **7127** for the Q channel modulator **7901b** by 90 degrees relative the control signals for the I channel modulator **7901a**. As a result, the Q modulator **7901b** samples the Q baseband signal **8004** with a 90 degree delay relative to the sampling of the I baseband signal **8002** by the I channel modulator **7901a**. Therefore, the Q harmonically rich signal **8008** is phase shifted by 90 degrees relative to the I harmonically rich signal **8006**. Since the phase shift is achieved using the control signals, an in-phase signal combiner **8206** combines the harmonically rich signals **8006** and **8008**, to generate the harmonically rich signal **8011**.

FIG. **83** illustrates a transmitter **8300** that is similar to transmitter **8200** in FIG. **82**. The difference being that the transmitter **8300** has a balanced modulator **8302** that utilizes a summing node **8304** to sum the I harmonically rich signal **8006** and the Q harmonically rich signal **8008** instead of the in-phase signal combiner **8206** that is used in the modulator **8202** of transmitter **8200**. The 90 degree phase shift between the I and Q channels is implemented by delaying the Q clock signals using 90 degree delays **8204**, as shown.

#### 7.3.2.3 IQ Transmitters Configured for Carrier Insertion

The transmitters **7420** (FIG. **74**) and **7608** (FIG. **76A**) have a balanced configuration that substantially eliminates any DC offset and results in minimal carrier insertion in the IQ output signal **7418**. Minimal carrier insertion is generally desired for most applications because the carrier signal carries no information and reduces the overall transmitter efficiency. However, some applications require the received signal to have sufficient carrier energy for the receiver to extract the carrier for coherent demodulation. In support thereof, FIG. **77** illustrates a transmitter **7702** to provide any necessary carrier insertion by implementing a DC offset between the two sets of sampling UFT modules.

Transmitter **7702** is similar to the transmitter **7420** with the exception that a modulator **7704** in transmitter **7702** is configured to accept two DC reference voltages so that the I channel modulator **7104a** can be biased separately from the Q channel modulator **7104b**. More specifically, modulator **7704** includes a terminal **7706** to accept a DC voltage reference **7707**, and a terminal **7708** to accept a DC voltage reference **7709**. Voltage **7707** biases the UFT modules **7124a** and **7128a** in the I channel modulator **7104a**. Likewise, voltage **7709** biases the UFT modules **7124b** and **7128b** in the Q channel modulator **7104b**. When voltage **7707** is different from voltage **7709**, then a DC offset will appear between the I channel modulator **7104a** and the Q channel modulator **7104b**, which results in carrier insertion in the IQ harmonically rich signal **7412**. The relative amplitude of the carrier frequency energy increases in proportion to the amount of DC offset.

FIG. **78** illustrates a transmitter **7802** that is a second embodiment of an IQ transmitter having two DC terminals to cause DC offset, and therefore carrier insertion. Transmitter **7802** is similar to transmitter **7702** except that the 90 degree phase shift between the I and Q channels is achieved by phase shifting the control signals, similar to that done in transmitter **7608**. More specifically, delays **7804a** and **7804b** phase shift the control signals **7123** and **7127** for the Q channel modulator **7104b** relative to those of the I channel modulator **7104a**. As a result, the Q modulator **7104b** samples the Q baseband signal **7404** with 90 degree delay relative to the sampling of the I baseband signal **7402** by the I channel modulator **7104a**. Therefore, the Q harmonically rich signal **7411b** is phase shifted by 90 degrees relative to the I harmonically rich signal **7411a**, which are combined by the in-phase combiner **7806**.

### 7.4 Transceiver Embodiments

Referring to FIG. **39**, in embodiments the receiver **3906**, transmitter **3910**, and LNA/PA **3904** are configured as a transceiver, such as but not limited to transceiver **9100**, that is shown in FIG. **91**.

Referring to FIG. **91**, the transceiver **9100** includes a diplexer **9108**, the IQ receiver **7000**, and the IQ transmitter **8000**. Transceiver **9100** up-converts an I baseband signal **9114** and a Q baseband signal **9116** using the IQ transmitter **8000** (FIG. **80**) to generate an IQ RF output signal **9106**. A detailed description of the IQ transmitter **8000** is included for example in section 7.3.2.2, to which the reader is referred for further details. Additionally, the transceiver **9100** also down-converts a received RF signal **9104** using the IQ Receiver **7000**, resulting in I baseband output signal **9110** and a Q baseband output signal **9112**. A detailed description of the IQ receiver **7000** is included in section 7.2.2, to which the reader is referred for further details.

### 7.5 Demodulator/Modulator Facilitation Module

An example demodulator/modulator facilitation module **3912** is shown in FIGS. **47** and **48**. A corresponding BOM list is shown in FIGS. **49A** and **49B**.

An alternate example demodulator/modulator facilitation module **3912** is shown in FIGS. **50** and **51**. A corresponding BOM list is shown in FIGS. **52A** and **52B**.

FIG. **52C** illustrates an exemplary demodulator/modulator facilitation module **5201**. Facilitation module **5201** includes the following: de-spread module **5204**, spread module **5206**, de-modulator **5210**, and modulator **5212**.

For receive, the de-spread module **5204** de-spreads received spread signals **3926** and **3928** using a spreading code **5202**. Separate spreading codes can be used for the I and Q channels as will be understood by those skilled in the arts. The demodulator **5210** uses a signal **5208** to demodulate the de-spread received signals from the de-spread module **5204**, to generate the I baseband signal **3930a** and the Q baseband signal **3932a**.

For transmit, the modulator **5212** modulates the I baseband signal **3930b** and the Q baseband signal **3932b** using a modulation signal **5208**. The resulting modulated signals are then spread by the spread module **5206**, to generate I spread signal **3942** and Q spread signal **3944**.

In embodiments, the modulation scheme that is utilized is differential binary phase shift keying (DBPSK) or differential quadrature phase shift keying (DQPSK), and is compliant with the various versions of IEEE 802.11. Other modulation

schemes could be utilized besides DBPSK or DQPSK, as will be understood by those skilled in arts based on the discussion herein.

In embodiments, the spreading code **5202** is a Barker spreading code, and is compliant with the various versions of IEEE 802.11. More specifically, in embodiments, an 11-bit Barker word is utilized for spreading/de-spreading. Other spreading codes could be utilized as will be understood by those skilled in the arts based on the discussion herein.

#### 7.6 MAC Interface

An example MAC interface **3914** is shown in FIG. **45**. A corresponding BOM list is shown in FIGS. **46A** and **46B**.

In embodiments, the MAC **3918** and MAC interface **3914** supply the functionality required to provide a reliable delivery mechanism for user data over noisy, and unreliable wireless media. This is done this while also providing advanced LAN services, equal to or beyond those of existing wired LANs.

The first functionality of the MAC is to provide a reliable data delivery service to users of the MAC. Through a frame exchange protocol at the MAC level, the MAC significantly improves on the reliability of data delivery services over wireless media, as compared to earlier WLANs. More specifically, the MAC implements a frame exchange protocol to allow the source of a frame to determine when the frame has been successfully received at the destination. This frame exchange protocol adds some overhead beyond that of other MAC protocols, like IEEE 802.3, because it is not sufficient to simply transmit a frame and expect that the destination has received it correctly on the wireless media. In addition, it cannot be expected that every station in the WLAN is able to communicate with every other station in the WLAN. If the source does not receive this acknowledgment, then the source will attempt to transmit the frame again. This retransmission of frame by the source effectively reduces the effective error rate of the medium at the cost of additional bandwidth consumption.

The minimal MAC frame exchange protocol consists of two frames, a frame sent from the source to the destination and an acknowledgment from the destination that the frame was received correctly. The frame and its acknowledgment are an atomic unit of the MAC protocol. As such, they cannot be interrupted by the transmission from any other station. Additionally, a second set of frames may be added to the minimal MAC frame exchange. The two added frames are a request to send frame and a clear to send frame. The source sends a request to send to the destination. The destination returns a clear to send to the source. Each of these frames contains information that allows other stations receiving them to be notified of the upcoming frame transmission, and therefore to delay any transmission their own. The request to send and clear frames serve to announce to all stations in the neighborhood of both the source and the destination about the pending transmission from the source to the destination. When the source receives the clear to send from the destination, the real frame that the source wants delivered to the destination is sent. If the frame is correctly received at the destination, then the destination will return an acknowledgment, completing the frame exchange protocol. While this four way frame exchange protocol is a required function of the MAC, it may be disabled by an attribute in the management information base.

The second functionality of the MAC is to fairly control access to the shared wireless medium. It performs this function through two different access mechanisms: the basic

access mechanism, call the distribution coordination system function, and a centrally controlled access mechanism, called the point coordination function.

The basic access mechanism is a carrier sense multiple access with collision avoidance (CSMA/CA) with binary exponential backoff. This access mechanism is similar to that used for IEEE 802.3, with some variations. CSMA/CA is a "listen before talk" (LBT) access mechanism. In this type of access mechanism, a station will listen to the medium before beginning a transmission. If the medium is already carrying a transmission, then the station that listening will not begin its own transmission. More specifically, if a listening station detects an existing transmission in progress, the listening station enters a transmit deferral period determined by the binary exponential backoff algorithm. The binary exponential backoff mechanism chooses a random number which represents the amount of time that must elapse while there are not any transmission. In other words, the medium is idle before the listening station may attempt to begin its transmission again. The MAC may also implement a network allocation vector (NAV). The NAV is the value that indicates to a station that amount of time that remains before a medium becomes available. The NAV is kept current through duration values that are transmitted in all frames. By examining the NAV, a station may avoid transmitting, even when the medium does not appear to be carrying a transmission in the physical sense.

The centrally controlled access mechanism uses a poll and response protocol to eliminate the possibility of contention for the medium. This access mechanism is called the point coordination function (PCF). A point coordinator (PC) controls the PCF. The PC is always located in an AP. Generally, the PCF operates by stations requesting that the PC register them on a polling list, and the PC then regularly polls the stations for traffic while also delivering traffic to the stations. With proper planning, the PCF is able to deliver near isochronous service to the stations on the polling list.

The third function of the MAC is to protect the data that it delivers. Because it is difficult to contain wireless WLAN signals to a particular physical area, the MAC provides a privacy service, called Wired Equivalent Privacy (WEP), which encrypts the data sent over the wireless medium. The level of encryption chosen approximates the level of protection data might have on a wireless LAN in a building with controlled access that prevents physically connecting to the LAN without authorization.

#### 7.7 Control Signal Generator—Synthesizer

In an embodiment, the control signal generator **3908** is preferably implemented using a synthesizer. An example synthesizer is shown in FIG. **55**. A corresponding BOM list is shown in FIGS. **56A** and **56B**.

#### 7.8 LNA/PA

An example LNA/PA **3904** is shown in FIGS. **64** and **65**. A corresponding BOM list is shown in FIG. **66**.

Additionally, FIG. **93** illustrates a LNA/PA module **9301** that is another embodiment of the LNA/PA **3904**. LNA/PA module **9301** includes a switch **9302**, a LNA **9304**, and a PA **9306**. The switch **9302** connects either the LNA **9304** or the PA **9306** to the antenna **3903**, as shown. The switch **9302** can be controlled by an on-board processor that is not shown.

#### 8.0 802.11 PHYSICAL LAYER CONFIGURATIONS

The 802.11 WLAN standard specifies two RF physical layers: frequency hopped spread spectrum (FHSS) and direct

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sequence spread spectrum (DSSS). The invention is not limited to these specific examples. Both DSSS and FHSS support 1 Mbps and 2 Mbps data rates and operate in the 2.400-2.835 GHz band for wireless communications in accordance to FCC part 15 and ETSI-300 rules. Additionally, 802.11 has added an 11 Mbps standard that operates at 5 GHz and utilizes OFDM modulation.

The DSSS configuration supports the 1 MBPS data rate utilizing differential binary phase shift keying (DBPSK) modulation, and supports 2 MBPS utilizing differential quadrature phase shift keying modulation. In embodiments, an 11-bit Barker word is used as the spreading sequence that is utilized by the stations in the 802.11 network. A Barker word has a relatively short sequence, and is known to have very good correlation properties, and includes the following sequence: +1, -1, +1, +1, -1, +1, +1, +1, -1, -1, -1. The Barker word used for 802.11 is not to be confused with the spreading codes used for code division multiple access (CDMA) and global positioning system (GPS). CDMA and GPS use orthogonal spreading codes, which allow multiple users to operate on the same channel frequency. Generally, CDMA codes have longer sequences and have richer correlation properties.

During transmission, the 11-bit barker word is exclusive-ored (EX-OR) with each of the information bits using a modulo-2 adder, as illustrated by modulo-2 adder 9202 in FIG. 92. Referring to FIG. 92, the 11-bit (at 11 MBPS) Barker word is applied to a modulo-2 adder together with each one (at 1 MBPS) of the information bits (in the PPDU data). The Ex-OR function combines both signals by performing a modulo-2 addition of each information bit with each Barker bit (or chip). The output of the modulo-2 adder results in a signal with a data rate that is 10× higher than the information rate. The result in the frequency domain signal is a signal that is spread over a wider bandwidth at a reduced RF power level. At the receiver, the DSSS signal is convolved with an 11-bit Barker word and correlated. As shown in FIG. 92, the correlation recovers the information bits at the transmitted information rate, and the undesired interfering in-band signals are spread out-of-band. The spreading and despreading of narrowband to wideband signal is commonly referred to as processing gain and is measured in decibels (dB). Processing gain is the ratio of DSSS signal rate information rate. In embodiments, the minimum requirement for processing gain is 10 dB.

The second RF physical layer that is specified by the IEEE 802.11 standard is frequency hopping spread spectrum (FHSS). A set of hop sequences is defined in IEEE 802.11 for use in the 2.4 GHz frequency band. The channels are evenly spaced across the band over a span of 83.5 MHz. During the development of IEEE 802.11, the hop sequences listed in the standard were pre-approved for operation in North America, Europe, and Japan. In North America and Europe (excluding Spain and France), the required number of hop channels is 79. The number of hopped channels for Spain and France is 23 and 35, respectively. In Japan, the required number of hopped channels is 23. The hopped center channels are spaced uniformly across the 2.4 GHz frequency band occupying a bandwidth of 1 MHz. In North America and Europe (excluding Spain and France), the hopped channels operate from 2.402 GHz to 2.480 GHz. In Japan, the hopped channels operate from 2.447 GHz to 2.473 GHz. The modulation scheme called out for FHSS by 802.11 is 2-level Gaussian Phase Shift Keying (GFSK) for the 1 MBps data rate, and 4-level GFSK for the 2 MBps data rate.

In addition to DSSS and FHSS RF layer standards, the IEEE 802.11 Executive Committee approved two projects for

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higher rate physical layer extensions. The first extension, IEEE 802.11a defines requirements for a physical layer operating in the 5.0 GHz frequency band, and data rates ranging from 6 MBps to 54 MBps. This 802.11a draft standard is based on Orthogonal Frequency Division Multiplexing (OFDM) and uses 48 carriers as a phase reference (so coherent), with 20 MHz spacing between the channels. The second extension, IEEE 802.11b, defines a set of physical layer specifications operating in the 2.4 GHz ISM frequency band. This 802.11b utilizes complementary code keying (CCK), and extends the data rate up to 5.5 Mbps and 11 Mbps.

The transmitter and receiver circuits described herein can be operated in all of the WLAN physical layer embodiments described herein, including the DSSS and FHSS embodiments described herein. However, the present invention is not limited to being operated in WLAN physical layer embodiments that were described herein, as the invention could be configured in other physical layer embodiments.

FIG. 94 illustrates a block diagram of an IEEE 802.11 DSSS radio transceiver 9400 using UFT Zero IF technology. DSSS transceiver 9400 includes: antenna 9402, switch 9404, amplifiers 9406 and 9408, transceivers 9410, baseband processor 9412, MAC 9414, bus interface unit 9416, and PCMCIA connector 9418. The DSSS transceiver 9400 includes an IQ receiver 7000 and an IQ transmitter 8000, which are described herein. UFT technology interfaces directly to the baseband processor 9412 of the physical layer. In the receive path, the IQ receiver 7000 transforms a 2.4 GHz RF signal-of-interest into I/Q analog baseband signals in a single step and passes the signals to the baseband processor 9412, where the baseband processor is then responsible for de-spreading and demodulating the signal. In embodiments, the IQ receiver 7000 includes all of the circuitry necessary for accommodating AGC, baseband filtering and baseband amplification. In the transmit path, the transmitter 8000 transforms the I/Q analog baseband signals to a 2.4 GHz RF carrier directly in a single step. The signal conversion clock is derived from a single synthesized local oscillator (LO) 9420. The selection of the clock frequency is determined by choosing a sub-harmonic of the carrier frequency. For example, a 5th harmonic of 490 MHz was used, which corresponds to a RF channel frequency of 2.450 GHz. Using UFT technology simplifies the requirements and complexity of the synthesizer design.

## 9. APPENDIX

The attached Appendix contained in FIGS. 95A-C, 96-161, which forms part of this patent application, includes schematics of an integrated circuit (IC) implementation example of the present invention. This example embodiment is provided solely for illustrative purposes, and is not limiting. Other embodiments will be apparent to persons skilled in the relevant art(s) based on the teachings herein. FIG. 95A illustrates a schematic for a WLAN modulator/demodulator IC according to embodiments of the invention. FIGS. 95B and 95C illustrate an expanded view of the circuit in FIG. 95A. FIGS. 96-161 further illustrate detailed circuit schematics of the WLAN modulator/demodulator integrated circuit.

## 10. CONCLUSIONS

Example implementations of the systems and components of the invention have been described herein. As noted elsewhere, these example implementations have been described for illustrative purposes only, and are not limiting. Other implementation embodiments are possible and covered by

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the invention, such as but not limited to software and software/hardware implementations of the systems and components of the invention. Such implementation embodiments will be apparent to persons skilled in the relevant art(s) based on the teachings contained herein.

While various application embodiments of the present invention have been described above, it should be understood that they have been presented by way of example only, and not limitation. Thus, the breadth and scope of the present invention should not be limited by any of the above-described exemplary embodiments, but should be defined only in accordance with the following claims and their equivalents.

What is claimed is:

1. A wireless modem apparatus, comprising:  
a balanced transmitter for up-converting a baseband signal, said balanced transmitter including,  
an inverter, to receive said baseband signal and generate an inverted baseband signal;  
a first controlled switch, coupled to a non-inverting output of said inverter, said first controlled switch to sample said baseband signal according to a first control signal, resulting in a first harmonically rich signal;  
a second controlled switch, coupled to an inverting output of said inverter, said second controlled switch to sample said inverted baseband signal according to a second control signal, resulting in a second harmonically rich signal; and  
a combiner, coupled to an output of said first controlled switch and an output of said second controlled switch, said combiner to combine said first harmonically rich signal and said second harmonically rich signal, resulting in a third harmonically rich signal.
2. The wireless modem apparatus of claim 1, wherein the first control signal and second control signal are phase shifted with respect to each other.
3. The wireless modem apparatus of claim 2, wherein the first control signal and the second control signal are phase shifted by 180 degrees relative to each other.
4. The wireless modem apparatus of claim 1, wherein the first control signal and the second control signal are configured to improve energy transfer to a desired harmonic of the third harmonically rich signal.
5. The wireless modem apparatus of claim 4, wherein a pulse width of the first control signal and the second control signal is configured to improve energy transfer to a desired harmonic of the third harmonically rich signal.
6. The wireless modem apparatus of claim 1, wherein the first control signal and the second control signal have a sampling frequency derived from a master clock signal of the balanced transmitter.
7. The wireless modem apparatus of claim 6, wherein said sampling frequency is equal to a sub-harmonic of the third harmonically rich signal.
8. The wireless modem apparatus of claim 6, wherein the first harmonically rich signal and the second harmonically rich signal each includes a plurality of harmonic images, repeating at harmonics of said sampling frequency.

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9. The wireless modem apparatus of claim 8, wherein the relative amplitude of said plurality of harmonic images is a function of a pulse width of the first control signal and the second control signal.

10. The wireless modem apparatus of claim 8, wherein the relative amplitude of a particular harmonic image of said plurality of harmonic images can be adjusted by adjusting said pulse width of the first control signal and the second control signal.

11. The wireless modem apparatus of claim 8, wherein energy transfer into higher frequency harmonics of said plurality of harmonic images is increased by reducing said pulse width of the first control signal and the second control signal.

12. The wireless modem apparatus of claim 8, wherein energy transfer into lower frequency harmonics of said plurality of harmonic images is increased by increasing said pulse width of the first control signal and the second control signal.

13. The wireless modem apparatus of claim 1, wherein said balanced transmitter further comprises:

a control signal generator that generates the first control signal and the second control signal.

14. The wireless modem apparatus of claim 1, wherein the third harmonically rich signal includes multiple harmonic images, wherein each of said images contains the baseband information of the baseband signal.

15. The wireless modem apparatus of claim 14, wherein said balanced transmitter further comprises:

a bandpass filter that selects for transmission one or more harmonic images of interest from said multiple harmonic images.

16. A method for up-converting a baseband signal, comprising:

receiving a baseband signal at an inverter;  
inverting said baseband signal to generate an inverted baseband signal;

sampling said baseband signal according to a first control signal to generate a first harmonically rich signal;

sampling said inverted baseband signal according to a second control signal to generate a second harmonically rich signal; and

combining said first harmonically rich signal and said second harmonically rich signal to generate a third harmonically rich signal.

17. The method of claim 16, wherein the first control signal and the second control signal are configured to improve energy transfer to a desired harmonic of the third harmonically rich signal.

18. The method of claim 16, wherein a pulse width of the first control signal and the second control signal is configured to improve energy transfer to a desired harmonic of the third harmonically rich signal.

19. The method of claim 16, wherein the first harmonically rich signal and the second harmonically rich signal each includes a plurality of harmonic images, repeating at harmonics of a sampling frequency of the first control signal and the second control signal.

20. The method of claim 19, wherein the relative amplitude of a particular harmonic image of said plurality of harmonic images can be adjusted by adjusting a pulse width of the first control signal and the second control signal.

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